PRINCIPLES OF RADIO

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PREFACE TO THE FIRST EDITION

Third Printing Revised

THIS textbook on radio has been written for those who must study without a teacher as well as for those who attend schools where courses in radio are given. Every attempt has been made to illustrate it with problems and examples which are practical in nature; they deal with the values of electrical constants which the radio engineer encounters. The experiments have been planned to give the "feel" of the apparatus that the research engineer or experimenter uses.

The radio art moves forward rapidly and at times unexpectedly. In this printing will be found material on tubes which have made their appearance since the book was first published, a new and simpler discussion of detection, and some description of technical aspects, discussed in the first edition as only then in sight, are handled in a more thorough manner because they are now in general use.

The author desires to acknowledge his appreciation for the aid which Howard E. Rhodes has given him in gathering material for the text and for the aid which Robert S. Kruse rendered by reading and criticising the original manuscript. Photographs, drawings, and other material are included by permission of the General Radio Company, the Samson Mfg. Co., E. T. Cunningham, Inc., Proceedings of the Institute of Radio Engineers, and Proceedings of the Institute of Electrical Engineers.

March, 1931. THE AUTHOR.

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CHAPTER I

FUNDAMENTALS

No one can learn a great deal about the theory and practice of radio who does not also know a few fundamental facts about electricity, for radio is but one aspect of a much broader field, electrical engineering. And since electricity is but a movement of the smallest known bit of matter and energy, the electron, it is necessary that a study of electricity must be preceded by a slight knowledge of the electron.

1. The electron.—The entire universe is made up of various combinations of about ninety substances known as **elements.** These elements are composed of but two things, negative electrical charges known as **electrons**, and positive charges known as **protons.** The electrons are all alike. The only difference between copper and aluminum lies in the difference in the number and position of their electrical charges.

2. Charged bodies.—The term charge is used in various ways. A body on which there is an equal amount of negative and positive electricity is said to be in equilibrium; but if the body has an excess of either negative or positive electricity it is said to be **charged.** Sometimes the body itself is called a charge and of course may be referred to as a positive or a negative charge. If it has a great excess of either of the two kinds of electricity, it is said to be highly charged. In this condition it is in a state of very unstable equilibrium, and at the least chance some change will occur to bring the body into a state of greater equilibrium.

3. The laws of electrical charges.—These electrical charges obey simple laws: like charges, whether positive or negative, repel each other; unlike charges, that is, a positive and a negative charge, attract each other.. The more highly charged the bodies are the greater will be the repulsion or attraction. The closer together the charges are the greater will be the attraction or repulsion. Doubling the distance between two unlike charges divides their attraction by four. The greater the magnitude of the individual charges the greater is the attraction or repulsion; the greater the distance between the charges the less the attraction or repulsion.

Experiment 1-1. This experiment demonstrates the production of charged bodies by friction and the laws that control such charged bodies. Whenever

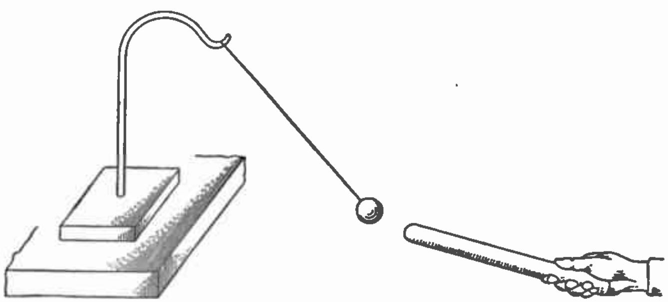


FIG. 1.—A familiar experiment in static electricity.

one body is rubbed by another, some frictional electricity is said to be generated. This amounts to stating that one of the bodies becomes charged. To get an appreciable charge, one needs a glass rod, a stick of sealing wax, a piece of silk and a piece of flannel, and a small bit of pith from a dry cornstalk or alder branch or sunflower stalk suspended as shown in Fig. 1 by means of a fine silk thread. Rub the piece of glass with the silk and bring near the pith ball; the pith ball should be repelled with considerable force. Then rub the wax stick with the flannel and bring it near the pith ball. It should be strongly attracted, proving that another kind of static or frictional electricity—or electrically charged body—has been generated. Now suspend two similar pith balls, touch one of them with the glass rod after rubbing it, and touch the other ball with the wax rod. Bring them near each other. Touch both balls with either the glass or the wax rod and bring them near each other. Now they are repelled. The latter part of the experiment is almost the starting point of the world's history of electrical experiment.

4. The atom.—The simplest form in which an element can exist by itself is called the atom. A combination of two or more atoms is called a molecule. Ordinarily the atom or molecule is in electrical equilibrium with its surroundings. If, however, through some severe mechanical shock for example, it should lose an electron it would be charged and then would follow the laws cited above. It would then attract or get rid of an electron at the first opportunity and become neutral again.

It is the motion of electrons that we know as the **electric current.** When there is a sufficient number of electrons, a billion billion per second, for instance, there is current enough to light an incandescent lamp or heat an electric iron.

The atoms and molecules in matter are in constant motion, carrying with them in their movements the electrons that constitute them; in the bumping of one atom against another, electrons are lost, gained, and interchanged.

Atoms of matter are inconceivably small. Everyone has seen many-colored oil films on the street. It is possible to obtain oil films less than half a ten-millionth of an inch thick. The atoms composing these films cannot be thicker than this figure; the electrons are much smaller yet. We think the distances in the solar system of which the earth is part are beyond comprehension, the sun for example being about 90 million miles from the earth; but the dimensions of the electrons in their smallness are even more difficult to picture. The diameter of the electron is estimated to be about 1 foot divided by a hundred million million. Each of these electrons resembles its brother exactly, so that when an electron is knocked out of an atom by a collision it is free to combine with any other body near by which may have a deficit of negative electricity, no matter what the body may be made of. The electron is the unit out of which everything is made.

5. The ether.—The fact that one charge can exert a force, either of attraction or repulsion, upon another implies that something connects the two. For instance, a comb which has been rubbed on the coat sleeve will pick up bits of paper even though it does not actually touch them, the paper jumping to the comb while the latter is still some distance from it. Evidently something exists in the space between the comb and the paper. That it is not air may be demonstrated by performing a similar experiment under a jar from which all the air has been pumped.

This leads us to a conception of what is commonly known as the **ether.** It is simply the place or the substance, or whatever one may choose to call it, wherein the attraction or repulsion of electrical charges exists. The ether is an invention made necessary by our difficulty in conceiving how one body can exert an effect upon another except through some intervening medium. Between two charged bodies are said to exist **lines of force** which tend to decrease the distance between the bodies if they are oppositely charged or to increase it if the bodies are charged alike. The sum of these lines of force is called an **electrical field** and every charged body is surrounded by such a field. Since a wireless aerial is but a charged system of wires it too has a field about it. This field extends in all directions through what we call the ether.

6. The electric current.—In an ordinary piece of copper wire the electrons are moving about in a haphazard fashion at the rate of about 35 miles per second. If this wire is in an electrical circuit, in addition to this to and fro motion there is a comparatively slow drift of electrons from one end of the wire to the other. It is this slow drift of electrons in a given direction that we ordinarily call the electric current. Because each electron can carry an extremely small quantity of electricity, it is only movements of large numbers of them that we are interested in. It has been estimated that it would take all the inhabitants of the earth, counting night and day at the highest rate of speed possible, 2 years to count the number of electrons which pass through an ordinary electric light in a second. This is about the same number that are necessary to light the tubes in a four-tube battery-operated receiver.

The flow of electrons from one end of the wire circuit to another can be explained by the two fundamental laws of electrical charges (Section 3). When a wire is attached to the positive terminal of a battery there is a momentary movement of the electrons nearest the end of the wire toward the battery. This movement soon ceases because the flow of electrons into the battery leaves a dearth of them at the other end of the wire which must be supplied. If both ends are attached to the battery a steady drift of electrons takes place out of the negative pole or terminal of the battery, through the wire, and to the battery again at the positive terminal.

Thus the actual motion of the electrons is from the negative toward the positive end of a circuit. This is in the opposite direction from the rule established many years before the electron had been discovered, namely, that current flows from positive to negative. In problems the student can assume either direction so long as he is consistent. We know that the electrons flow from negative to positive; electrical workers assume the current flows from positive to negative. In this book we shall follow the latter rule, but the student should remember that the actual carriers of electricity move in the opposite direction.

7. Insulators and conductors.—It is a matter of common knowledge that the current does not flow through the non-metallic parts of a radio set, or through the insulating material around a broken conductor. How does it happen that some materials are such good "conductors," copper and silver for example, whereas others, such as glass or bakelite, appear not to conduct at all? Here again we are dealing with the building stones of all matter, the atom and the electron. Atoms of the so-called non-conductors maintain their hold on their individual electrons very tightly; few electrons escape. In the conductors, the electrons of the various atoms are freer to move about, and so to be interchanged among atoms. A conductor is a substance that quickly loses its charge when rubbed. A non-conductor retains its charge longer.

A good conductor is a material whose electrons are freer to move about than those of a poor conductor. Strictly speaking, there are no non-conductors. All materials will carry current to some degree. Glass, for example, which is generally considered a very good insulator, conducts electricity fairly well when it is in a molten state.

The best insulators—that is, the poorest conductors—are amber, rubber, sulphur, shellac, porcelain, quartz, silk, air. Dry wood, paper, cotton and linen thread are semi-conductors. The best conductors are the metals, acids, moist earth, etc.

8. Conductivity.—All materials have a certain characteristic which we may call **conductivity,** which describes their ability to conduct an electric current. Among pure metals silver has a very high conductivity, copper is next, and near the bottom lies iron with about one-ninth the conductivity of copper. The **conductance** of a circuit is a term expressing its ability to pass an electric current. The greater the conductance, the greater the current.

9. Resistance.—Those metals which have a high conductivity may be said to offer little **resistance** to the flow of electrons through them. Thus, copper has a low resistance, while some combinations of copper, nickel, and iron-manganese, for example, have resistances many times that of copper. A device added to a circuit to increase its resistance is called a "resistor." The words resistance and resistor are used synonymously in this text.

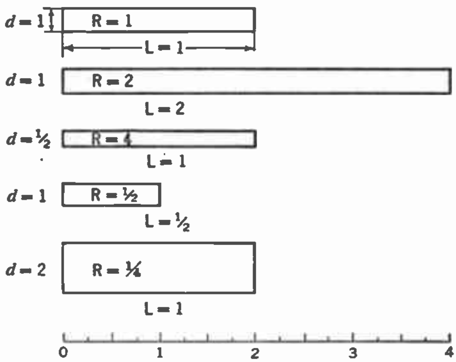


FIG. 2.—Resistance depends upon the length and size of a conductor.

The resistance of two wires of the same material and at the same temperature depends upon two things, the length of the wires and the area of their cross-section. Naturally, the longer the wire the fewer electrons can pass through it in a given time; similarly the smaller the diameter of a wire the greater the resistance, just as you can get more gallons of water per second from a 3-inch fire hose than from a 1-inch garden hose, although they may be attached to the same hydrant.

Similarly, a wire 2 feet long has twice the resistance of a wire 1 foot long but of the same diameter. Of two wires the same length the one having the smaller diameter will have the greater resistance. (See Fig. 2.)

The resistances of several metals compared to silver are as follows:

Silver	1.00	Platinum	7.20
Copper	1.11	German silver	14.20
Aluminum	1.87	Hard steel	13.5
Nickel	4.67	Mercury	63.1
Soft iron	6.00		

Problem 1–1. How many times higher in resistance is mercury than silver? Than copper?

Problem 2–1. Two wires of the same length and diameter have resistances in the ratio of 5.45 to 1. If the lower resistance wire is copper, could you identify the other wire material from the above table?

Problem 3–1. Two wires, one of soft iron and the other of hard steel, are to have the same resistance. They have the same diameter. The hard steel wire is one foot long. What is the length of the soft iron wire?

10. The ohm.—The unit of resistance is the ohm. It is the resistance of a column of mercury weighing 14.4521 grams, having a uniform cross-section and a height of 106.3 cm. at 0° Centigrade. A 9.35-foot length of No. 30 copper wire has a resistance of about one ohm. The table on page 17 gives sizes and resistance per thousand feet of copper wire. The resistance per foot may be obtained from such a table by dividing the resistance per thousand feet by one thousand.

Note that increasing the size of wire by three numbers, that is, from No. 20 to No. 23, doubles the resistance of the wire from 10.15 to 20.36 ohms; going from No. 30 to No. 27 lowers the resistance from 103.2 to 51.5 ohms per thousand feet.

Copper is used in electrical and radio circuits because of its high conductivity compared to other metals and its low cost compared to metals of higher conductivity. It is readily obtainable and easily worked.

Problem 4–1. What size of soft iron wire will have the same resistance as No. 32 copper?

Problem 5–1. What is the resistance of 1 foot of No. 20 copper? Of No. 24 hard steel?

Problem 6–1. What is the resistance of a column of mercury of the following dimensions, weight 0.032 lb. (1 pound = 453.6 grams), length 41.7 inches (1 inch = 2.54 centimeters) at 0° C., the column having uniform cross-section?

11. The effect of molecular motion on resistance.—Why do some substances have greater resistance than others? Let us again consider the electrons, atoms, and molecules which make up the wires carrying the currents. Not only are the electrons in motion, but the atoms and molecules themselves are in a sluggish motion, the violence of this motion depending upon the temperature of the wire and the material of which the wire is made.

And although molecules cannot traverse the electric circuit as the electrons can, in their to and fro motion they impede the progress of the electricity bearers by countless collisions with them. The greater this molecular motion, the greater the resistance to a progressive flow of electrons, and the greater the wire's electrical resistance.

12. The effect of temperature on resistance.—The resistance of all pure metals rises with increase in temperature. This is because of the greater molecular agitation at higher temperatures, making it more difficult for the electrons to drift in their progressive motion around the circuit.

At absolute zero, 273 degrees below zero Centigrade, all molecular motion is supposed to stop, making the resistances of metals practically zero. At the lowest temperature reached it has been found that the resistance of a coil of wire is so low that current will flow for some time after the driving force is removed. Absolute zero has not been reached up to the present time.

13. Temperature coefficient of resistance.—Conductors in which radio engineers are interested increase or decrease in resistance at a regular rate with respect to temperature. The change in resistance of a given wire may be computed from the following facts. The "temperature coefficient of resistance" is a term which gives the amount a resistance increases for each degree rise in temperature for each ohm at the original temperature. For example, if a copper wire with a temperature coefficient of 0.0042 has a resistance of 80 ohms at 0° C., this resistance will be increased by 80×0.0042 for each degree rise in temperature. At 50° C. the resistance increase would be $80 \times 0.0042 \times 50$ or 16.8 ohms, and the resistance would now be $80 + 16.8$ or 96.8 ohms. Manganin wire, composed of 84 per cent copper, 12 per cent manganese, 4 per cent nickel, has a very low temperature resistance. It is 0.000006. The change in resistance of two metals with temperature is shown in Fig. 3.

14. The ampere.—The ampere is the term used to express the rate at which electrons move past a given point in an electrical circuit. It is equal to 6.28×10^{18} (see Section 16) electrons per second. Since each electron carries a definite quantity of electricity, the total amount carried by 6.28×10^{18} electrons is a

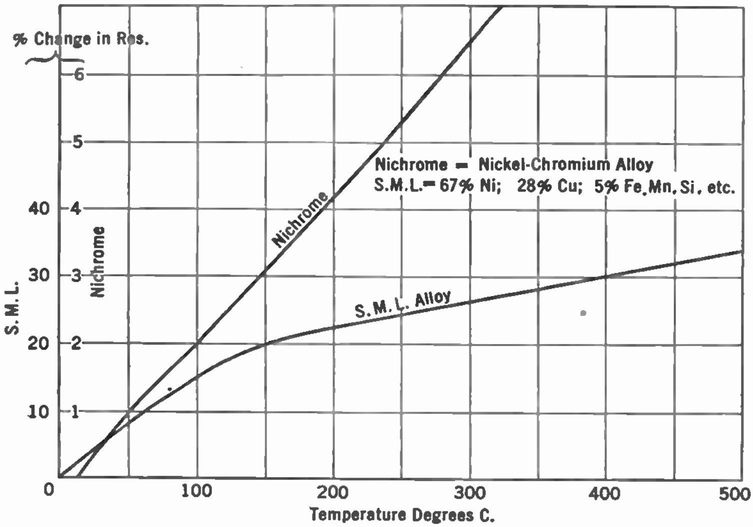


FIG. 3.—Effect of temperature on resistance.

definite quantity and is known as the coulomb. The ampere, however, is the term used in electrical practice. It corresponds to the term gallons per second used in speaking of the amount of water transported through a pipe or hose. The term gallons alone conveys little meaning, since the same number of gallons will flow out of a small hose as out of a large one provided we do not consider the time involved, or the pressure. But "gallons per second" involves both time and pressure and is a term easily visioned. A current of one ampere will convey through a circuit one coulomb of electricity per second.

The ampere as a quantity of electricity transported per second is a large unit if we compare it with the current flowing from the B batteries of a radio set. It is small compared with the currents encountered in power houses. The B batteries supply only thousandths of amperes or milliamperes, whereas in a small power house supplying power to a village one may have thousands of amperes flowing. A meter to measure the flow of current is called an ammeter, or milliammeter, or microammeter, depending upon the strength of current it can measure. Approximate currents flowing through commonly used devices are shown below.

Apparatus	Approximate Current in Amperes
50-watt lamp	0.5
250-watt lamp	2.5
2-horsepower motor	10
Electric iron	5
Filament of vacuum tube	0.25
Plate circuit of vacuum tube	0.001

15. The volt.—The electrons are driven through the wires and apparatus composing the circuit by a force called an **electromotive force**, abbreviated to e.m.f. The unit of force is known as the **volt.** It is the electrical force that will cause one ampere of electricity to flow through a wire which has one ohm of resistance. The common dry cell used to ring door bells has a voltage of about 1.5; storage batteries when charged have a voltage of about 2.0 and thus a three-cell battery has a voltage of 6.0. The ordinary B battery has a voltage of about 45, and if torn apart will be found to consist of 30 small cells, the voltage of which is 1.5 volts each. When the total voltage of such a battery is as low as 37 the battery should be thrown away. An instrument used to measure voltages is known as a voltmeter. A table of voltages is given below.

Apparatus	Voltage (Approximate)
Dry cell	1.5
Storage battery	6
B battery	45
House lighting circuit	115
"Third rail"	500

16. Engineers' shorthand.—Engineers have a simple shorthand method of working with large numbers well illustrated by the figures 6.28×10^{18}, which really means that 6.28 multiplied by a million million million electrons flowing past a given point per second constitute the electric current known as an ampere. We shall have occasion to use this system many times in the course of the book and students are encouraged to master it as soon as possible. The table below will be helpful.

$$1 = 10^0 = \text{one}$$
$$10 = 10^1 = \text{ten}$$
$$100 = 10^2 = \text{hundred}$$
$$1000 = 10^3 = \text{thousand, etc.}$$
$$1 = 10^0 = \text{one}$$
$$.1 = 10^{-1} = \tfrac{1}{10} = \text{one-tenth}$$
$$.01 = 10^{-2} = \tfrac{1}{100} = \text{one-hundredth}$$
$$.001 = 10^{-3} = \tfrac{1}{1000} = \text{one-thousandth, etc.}$$

The small number above the figure 10 is called the **exponent.** Numbers less than 1 have negative exponents. Thus three-thousandths may be expressed in these several ways:

$$.003 = 3 \times 10^{-3} = \frac{3}{1000} = \frac{3}{10^3}$$

When numbers are multiplied, their exponents are added; when the numbers are divided, the exponents are subtracted. Thus 100 multiplied by four-tenths may be done in shorthand as follows:

$$\begin{aligned} 100 \times .4 &= 10^2 \times 4 \times 10^{-1} \\ &= 4 \times 10^1 \\ &= 4 \times 10 \\ &= 40 \end{aligned}$$

Similarly, let us divide 3000 by 150.

$$\begin{aligned} 3000 \div 150 &= (3 \times 10^3) \div (1.5 \times 10^2) \\ &= \frac{3}{1.5} \times 10^3 \times 10^{-2} \\ &= 2 \times 10 \\ &= 20 \end{aligned}$$

The rules are few and those are simple:

1. To multiply, add exponents.
2. To divide, subtract exponents.
3. When any number crosses the line, change the sign of the exponent.

Example 1–1. Multiply 20,000 by 1200 and divide the result by 6000.

$$20{,}000 = 2 \times 10^4$$

$$1200 = 12 \times 10^2$$

$$6000 = 6 \times 10^3$$

$$\frac{20{,}000 \times 1200}{6000} = \frac{2 \times 10^4 \times 12 \times 10^2}{6 \times 10^3}$$

$$= \frac{2 \times 12 \times 10^4 \times 10^2 \times 10^{-3}}{6}$$

$$= \tfrac{24}{6} \times 10^3$$

$$= 4000$$

Problem 7–1. How many electrons flow past a given point per second when the number of amperes is 6? 60? 600? 0.1? 0.003?

Problem 8–1. The sun is roughly 90 million miles from the earth. Express this in "shorthand."

Problem 9–1. At 100 miles per hour, how many months would it take to reach the sun?

Problem 10–1. If light travels at 300 million meters per second and if a meter equals 3.3 feet, how long does it take the sun's rays to reach the earth?

Problem 11–1. How many amperes of current flow when 31.4×10^{15} electrons per second flow past a point?

In connection with such shorthand methods the following table of prefixes commonly used will be important.

Prefix	Abbreviation	Meaning
micro	μ	one millionth
milli	m	one thousandth
centi	c	one hundredth
deci	d	one tenth
deka	dk	ten
hekto	h	one hundred
kilo	k	one thousand
mega	M	one million

Thus a thousandth of an ampere is known as a milliampere, a million ohms is called a megohm, etc.; or, expressed in numbers, 1 milliampere = 10^{-3} or .001 ampere; 1 megohm = 1,000,000 ohms.

17. Mathematics in the study of radio.—The amount of mathematics one needs varies with the intensity with which one intends to study radio. As in all other branches of science in which mathematics plays a part the easier it is to think mathematically

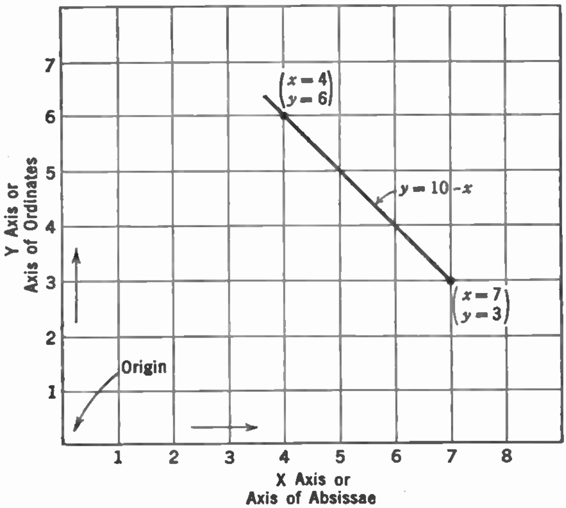


FIG. 4.—Curves are usually drawn with the origin as shown.

the greater are the possibilities ahead of the student. In this book it is necessary to have only a rudimentary knowledge of algebra to work most of the problems. The student with no mathematics beyond arithmetic and common sense will be able to work his way through most of the examples.

18. Curve plotting.—Many of the answers to radio problems can be seen visually if the problem is plotted in the form of a graph. Such graphs or curves are used frequently in this text, and it is essential that the student and experimenter not only shall be familiar with how to plot curves but how to interpret curves that other experimenters have drawn.

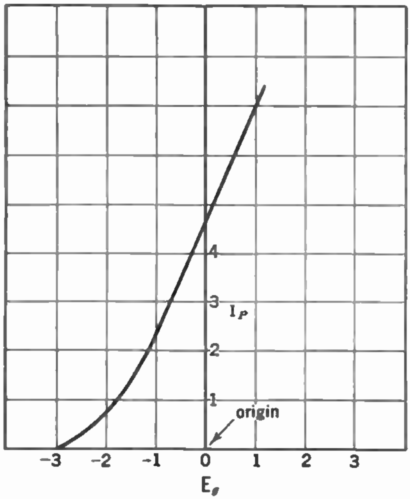


FIG. 5.—The origin in the center.

The simplest form of curve is a map. The map has two **co-ordinates** or **axes,** north-south and east-west. We say that a town is situated at so many miles east and so many miles south of some point that we take as the origin. We have now plotted the simplest mathematical equation, a point. A railroad runs straight north past a point, that is, so many miles east of this town. We can locate this railroad by giving two points through which it passes, or by giving one point through which it passes and its direction. By a point and a direction we have plotted the next simple mathematical equation, a straight line.

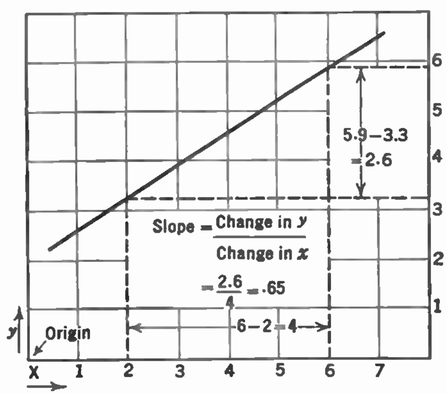


FIG. 6.—How to calculate the shape of a curve.

In radio plots the axes may be called X for the horizontal and Y for the vertical, or current for one and voltage for the other, etc. A graph is a visual expression of the relation existing between two factors, X and Y, or current and voltage, etc. When one increases the other increases or decreases. Knowing the law connecting them (the equation or formula, we call it) we can tell what the current is at any given voltage. If the law expressed visually in the form of a graph is a straight line, we say the two factors, current and voltage, are proportional. If one increases and the other decreases, we say they are inversely proportional.

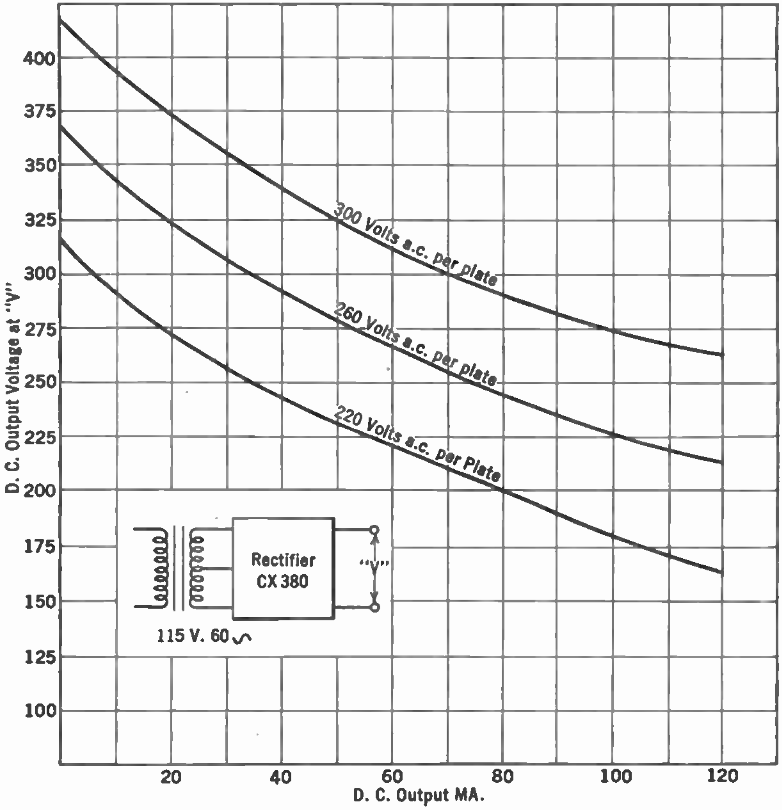


FIG. 7.—A "B eliminator" regulation curve.

Curves are useful not only in giving us a visual picture of what is happening in a circuit, but in telling us if the figures secured in an experiment are correct. Thus we may calibrate a wavemeter in condenser dial degrees against wavelength in meters. We plot this curve and one or more points do not seem to fall on the smooth curve that goes through the other points. Something in our laboratory experiment caused these points to be off the curve. They were incorrectly taken, and the measurement that gave us these points must be repeated.

The origin, sometimes, is at the lower left-hand corner of the curve, as in Fig. 4, although it may be in the center or somewhere else, as in Fig. 5, which shows the relation between the current in the plate circuit of a vacuum tube as it is controlled by the amount of voltage on the grid of that tube.

Points which lie to the left of the vertical axis are negative;

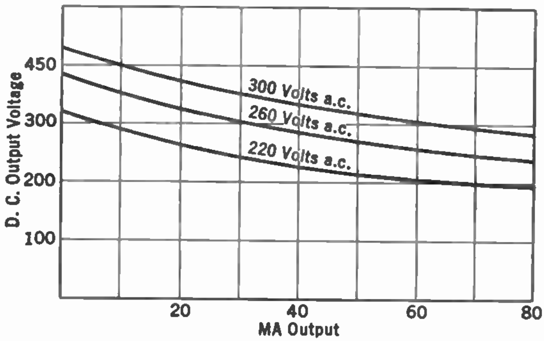


Fig. 8.—The same data as in Fig. 7 but to a different scale.—Note how much flatter the curves appear.

points which lie below the horizontal axis are negative. All others are positive.

The change in the vertical units with a given change in horizontal units is called the **slope** of the curve. If the curve goes through the origin this slope amounts to the ratio between the vertical and the horizontal values at any point. In Fig. 6 is shown the method of calculating the slope.

The units in which a curve is plotted change its appearance. Thus in Fig. 7 is plotted the relation between the output voltage of a " B eliminator " as the current taken by the receiver is changed. Figure 8 shows the same data but plotted to a different vertical scale. The slope of these lines looks different but really is the same. If the slope is the factor in which we are interested, the more open scale should be used so that small changes will be visible.

19. Symbols.—In all technical literature a number of abbreviations are used to express parts of circuits. For example, in very popular articles a "picture diagram" may be used, but picture diagrams are only for the boy and the experimenter who are too lazy or disinterested to learn radio language. The symbols used in this book are shown on the next two pages. A circuit is built up simply by connecting several of these symbols together.

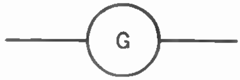
Copper Wire Tables

Resistance at 68° F. (20° C.)

Mils, .001 inch

Size of Wire B. & S. Gauge	Diameter of Wire Mils.	Ohms per 1000 Ft.	Pounds per 1000 Ft.	Turns per Linear Inch			
				S.c.c.	D.c.c.	S.s.c.	D.s.c.
0000	460	.049	641	2.14	2.10		
000	410	.0618	508	2.39			
00	365	.0779	403	2.68	2.62		
0	325	.0983	319	3.00			
1	289	.1239	253	3.33	3.25		
2	258	.1563	201	3.75			
3	229	.1970	159	4.18	4.03		
4	204	.2485	126	4.67			
5	182	.3133	100	5.21	5.00		
6	162	.3951	79.5	5.88			
7	144	.4982	63	6.54	6.25		
8	128	.6282	50.0	7.35			
9	114	.7921	39.6	8.26	7.87		
10	102	.9989	31.4	9.25			
11	91	1.260	24.9	10.3	9.80		
12	81	1.588	19.8	11.5			
13	72	2.003	15.7	12.8	12.2		
14	64	2.525	12.4	14.3			
15	57	3.184	9.86	15.9	14.9		
16	51	4.016	7.82	17.9	16.7	18.9	18.3
17	45	5.064	6.20	20.0			
18	40	6.385	4.92	22.2	20.4	23.6	22.7
19	36	8.051	3.90	24.4			
20	32	10.15	3.09	27.0	24.4	29.4	28.0
21	28.5	12.80	2.45	29.9			
22	25.3	16.14	1.94	33.9	30.0	36.6	34.4
23	22.6	20.36	1.54	37.6			
24	20.1	25.67	1.22	41.5	35.6	45.3	41.8
25	17.9	32.37	.97	45.7			
26	15.9	40.81	.769	50.2	41.8	55.9	50.8
27	14.2	51.47	.610	55.0			
28	12.6	64.90	.484	60.2	48.6	68.5	61.0
29	11.3	81.83	.384	65.4			
30	10.0	103.2	.304	71.4	55.6	83.3	72.5
31	8.9	130.1	.241	77.5			
32	8.0	164.1	.191	83.4	62.9	101	84.8
33	7.1	206.9	.152	90.0			
34	6.3	260.9	.120	97.1	70.0	121	99.0
35	5.6	329.0	.0954	104			
36	5.0	414.8	.0757	111	77.0	143	114
37	4.5	523.1	.0600	118			
38	4.0	659.6	.0476	125	83.3	167	128
39	3.5	831.8	.0377	135			
40	3.1	1049	.0299	141	90.9	196	145

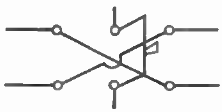
Headphones



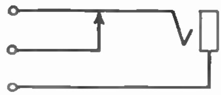
Galvanometer

Key

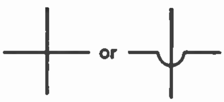
Wires Connected



Reversing Switch



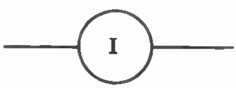
Closed Circuit Jack



Wires crossed
but not Connected

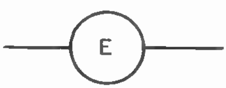
Single Pole
Double Throw Switch
"S.P.D.T."

L = Inductance
C = Capacity
R = Resistance
ω = Ohms
-Ω- = Megohms
mH = Millihenries
Mfd. = Microfarads
Mmfd. = Micro Microfarads
μH = Microhenries

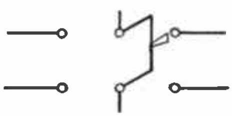


Ammeter or
Milliammeter

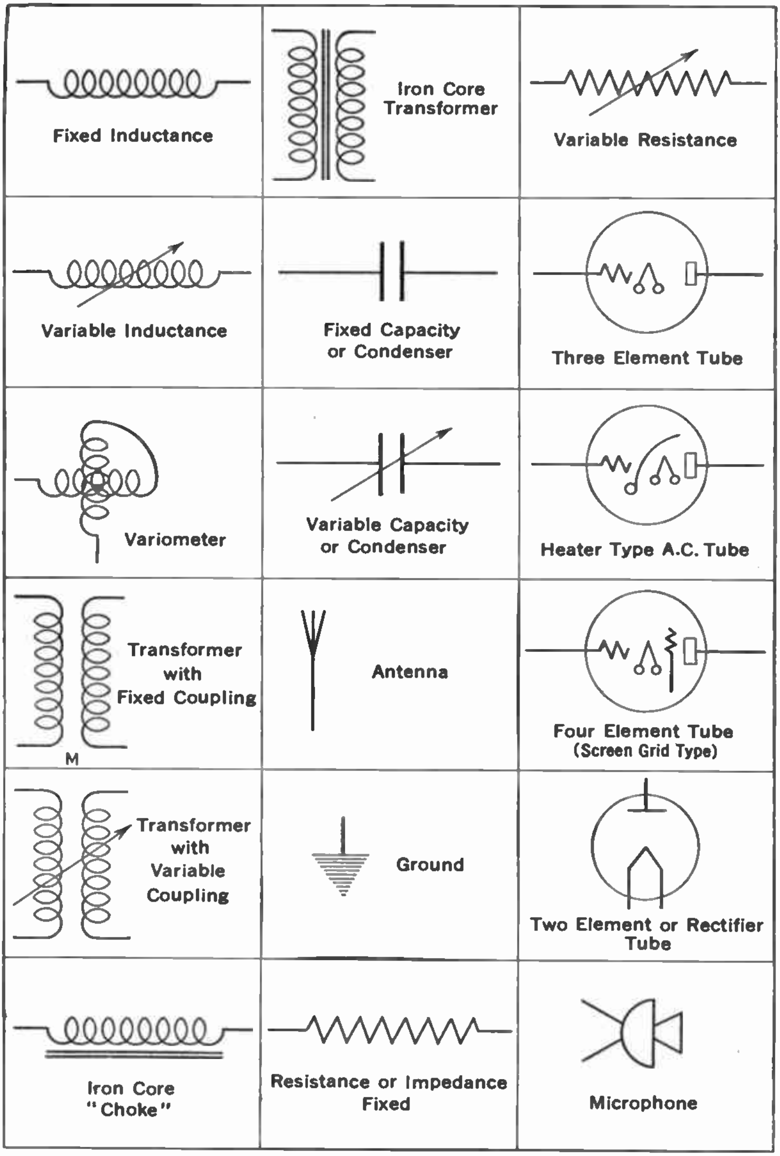
"S.P.S.T." Switch



Voltmeter



Double Pole
Double Throw Switch
"D.P.D.T."


Fixed Inductance
Iron Core Transformer
Variable Resistance
Variable Inductance
Fixed Capacity or Condenser
Three Element Tube
Variometer
Variable Capacity or Condenser
Heater Type A.C. Tube
Transformer with Fixed Coupling
M
Antenna
Four Element Tube (Screen Grid Type)
Transformer with Variable Coupling
Ground
Two Element or Rectifier Tube
Iron Core "Choke"
Resistance or Impedance Fixed
Microphone

CHAPTER II

OHM'S LAW

In the previous chapter we stated that an electric current was a motion of electrons; that the force which caused the motion of the electrons was called an electromotive force (e.m.f.) or a potential difference (p.d.), that the resistance of a circuit opposes the flow of current, and that the unit of the current which actually flows per second is called the ampere. We have then a very simple law which enables the engineer to calculate

1. The current that will flow when the voltage and resistance are known.

2. The voltage necessary to force a certain amount of current through a known resistance.

3. The resistance that will restrict the current to a certain value under pressure of a certain e.m.f. expressed in volts.

20. Ohm's law.—The law which governs all simple and many complex electrical phenomena is known as **Ohm's law.** This law states that: Current in amperes equals e.m.f. in volts divided by resistance in ohms, or, as expressed in electrical abbreviations,

$$I \text{ (current)} = \frac{E \text{ (voltage)}}{R \text{ (resistance)}}.$$

21. Ways of Stating Ohm's law.—There are three ways of stating this fundamental law. They are:

(1) $I = E/R$ (2) $E = I \times R$ (3) $R = E/I$

These three ways of stating the same law are determined from the first statement of Ohm's law by simple mathematical transformation, and make less difficult the solving of problems.

22. Voltage drop.—The second way of stating Ohm's law is that whenever a current flows through a resistance, there is a difference of potential at the two ends of that resistance. For every ampere of current that flows through an ohm of resistance, there is a volt lost. In other words it requires a volt to force an ampere through an ohm of resistance, and once that task is over, the volt is gone.

Consider Fig. 9, which shows the voltage-divider between a radio receiver and a voltage supply system for feeding power to the receiver. The power tube may require 180 volts. Other tubes require only 90 volts or perhaps small negative voltages. If 20 milliamperes of current flow through this voltage-divider, whose resistance may be 5000 ohms, and if there are 180 volts across the entire resistance, there will be other voltages along the resistance as indicated in the illustration. If the negative terminal of a voltmeter were attached to the negative end of the voltage-divider and the positive terminal of the meter touched to various points along the resistance on the way toward the positive end, greater and greater voltages would be measured. What is being measured at each point is the drop in voltage between that point and the negative terminal of the voltage-divider.

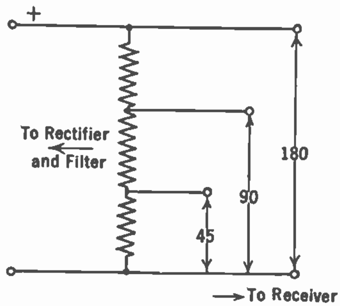


Fig. 9.—The voltage divider of a receiver's power apparatus.

Often in laboratories a voltage is needed so small that it cannot be measured with available instruments. A larger voltage can be measured easily, however; and if it is impressed across a voltage-divider, any desired part of the total voltage may be utilized by tapping into this divider. (See Problem 4–2.)

These voltages appearing across a resistance because of current flowing through that resistance are known as *IR* drops. They may be calculated by multiplying the resistance in ohms by the current in amperes.

Example 1-2. In Fig. 10 is an " output choke " coupling a loud speaker to a power tube. The tube requires that 180 volts shall be impressed between its plate terminal and its negative filament terminal. The question is, how many volts must the B battery have in order to impress this voltage on the tube?

The plate current is 18 milliamperes. The d.-c. resistance of the choke coil is 1700 ohms. The voltage used up in forcing 18 milliamperes through the 1700 ohms is 30.6. This voltage never gets to the tube. The voltage measured between plate and negative filament will be the B battery voltage minus the *IR* drop across the choke. Hence the total voltage required is 180 for the tube and 30.6 for the choke, or 210.6 volts. One of the requirements of a good choke for such purposes is that it have a low d.-c. resistance. Otherwise too much voltage is lost there.

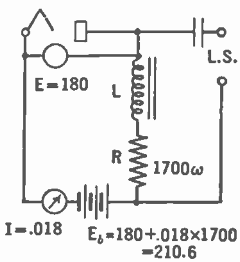


FIG. 10.—A choke-condenser coupling circuit.

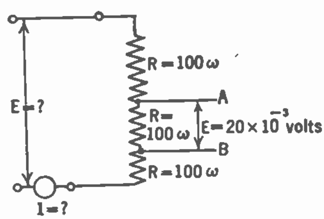


FIG. 11.—Use of an *IR* drop as a source of voltage.

Problem 1-2. What current flows through a vacuum tube filament connected to a 5-volt battery if its resistance is 20 ohms?

Problem 2-2. Suppose we desire to limit to 1 milliampere the flow of current in a circuit attached to a 45-volt B battery. What must be the total resistance of the circuit?

Problem 3-2. How much voltage is required to force a current of 60 milliamperes through a tube whose filament resistance is 50 ohms?

Problem 4-2. Consider Fig. 11. How many milliamperes of current must be forced through the circuit in order to get 20 millivolts across the resistor *A-B*? How many volts in all will be needed?

23. Graphs of Ohm's law.—An interesting study of Ohm's law may be made by means of the circuit shown in Fig. 12 and several sheets of plotting or graph paper. The result of plotting current against voltage with constant resistance (Fig. 13); or resistance against current with constant voltage (Fig. 14); or

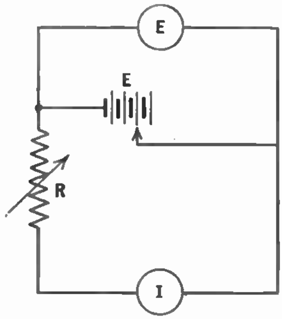


FIG. 12.—A circuit for testing Ohm's law.

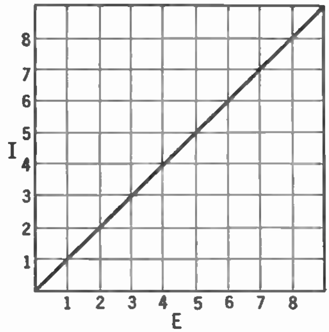


FIG. 13.—In an Ohm's law circuit plotting current against voltage results in a straight line.

voltage against resistance with constant current—all give an accurate graphical picture of what Ohm's law means. In Chapter I the term conductance, K, was defined. It is equal to $1/R$. When conductance against current is plotted, a straight line results, as shown in Fig. 15. When voltage and current are plotted with a fixed resistance in the circuit, the curve is a straight line if the circuit follows Ohm's law.

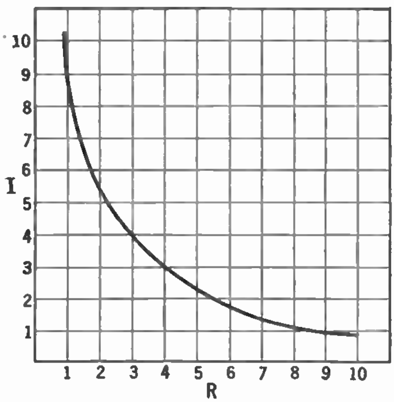


FIG. 14.—The result of plotting current against resistance.

Experiment 1-2. If the apparatus is at hand, connect it up as in Fig. 12, using a 6-volt battery, a 40-ohm rheostat, and an ammeter reading a maximum of about 0.5 ampere. Connect the maximum resistance in the circuit and note the current as the voltage is changed from 2 to 4 and then 6 volts by tapping onto each of the three cells of the storage battery. Plot the data. Then use a smaller value of resistance and repeat.

Then use 2 volts and adjust the rheostat until several current readings have been obtained. Calculate from Ohm's law what the resistance is and plot resistance against current.

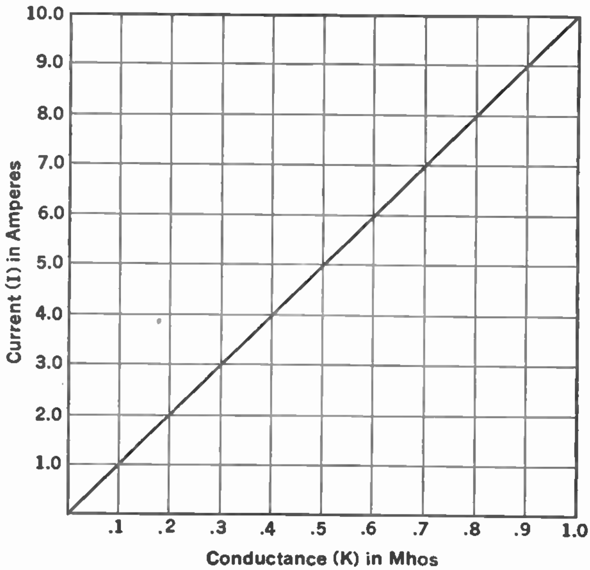


Fig. 15.—Conductance $\left(\frac{1}{R}\right)$ plotted against current.

Convert the resistances into conductances and plot against current. Calculate similar data, using 4 volts and then 6 volts, and plot the data.

Note in each case the shape of the curve has not changed, although the slopes of the straight lines vary with the resistance and the curved lines are displaced from each other.

Problem 5-2. Plate current (20 ma.) flows through R in Fig. 16. What must be the resistance in order to make the grid of the tube 40 volts more negative than the cathode? There is no loss in voltage in the coil.

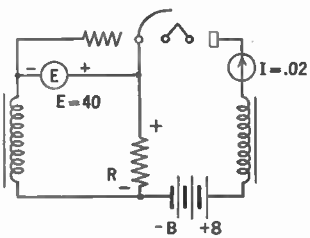


Fig. 16.—A problem in Ohm's law—to determine the value of R to provide bias for grid of tube.

24. Series and parallel circuits.—There are two ways in which electrical apparatus may be connected together.

When two or more pieces of equipment are connected as in Fig. 17 they are said to be in series. The same current flows through each unit. The voltage drop across each unit is controlled by its resistance, and if one of these units has twice the resistance of the other, the voltage drop across it will be twice as great. The sum of the voltage drops across the three resistances must be equal to the voltage of the battery, for there is no other place in the circuit for the voltage to be used.

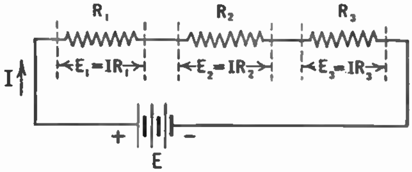


FIG. 17.—A simple series circuit.

In a series circuit the total resistance is the sum of the individual resistances. The current in each unit is the same as in all other units. The current is obtained from Ohm's law (1).

If any of the units becomes " open " the current ceases to flow. If, however, any unit becomes " shorted " the current will increase because the total resistance of the circuit has decreased.

Example 2-2. In Fig. 18 is a typical series circuit composed of a vacuum tube of the 201-A type which has a filament resistance of 20 ohms, a 6-volt battery, a current meter, and a rheostat or variable resistor whose purpose is to limit the flow of current through the filament of the tube. Note also Fig. 19 in which the same circuit is represented using electrical symbols. The arrow through R_1 indicates that it can be adjusted in value. R_2 indicates the resistance of the filament.

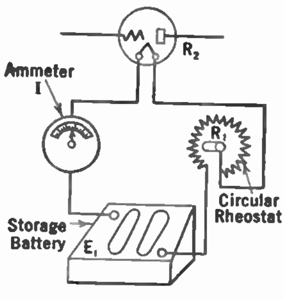


FIG. 18.—A series circuit used in radio apparatus.

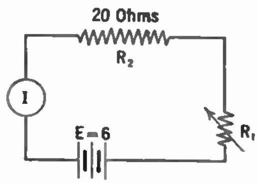


FIG. 19.—The equivalent of Fig. 18.

The question is, what current will flow through the circuit as the resistance of R_1 is varied? Suppose it is 4 ohms. We know the same current will flow through both the filament and the rheostat. The resistance, then, in the circuit is equal to 20 plus 4 or 24 ohms, and by Ohm's law we know that the current will be the voltage divided by the total resistance, or

$$I = \frac{E}{R_1 + R_2}$$

$$= \frac{6}{4 + 20} = \frac{6}{24} = 0.25 \text{ ampere.}$$

There are two resistances in this circuit. Current flows through them. There must then be two voltage drops. Let us calculate what they are. By equation 2 we multiply the resistance by the current.

$$\text{voltage drop} = IR_1 = .25 \text{ ampere} \times 4 \text{ ohms} = 1 \text{ volt}$$
$$\text{voltage drop} = IR_2 = .25 \text{ ampere} \times 20 \text{ ohms} = 5 \text{ volts}$$

In other words, of the six volts available at the terminals of the battery, five have been used up across the 20-ohm resistance and one volt has been used to drive 0.25 ampere through the 4-ohm resistance.

Problem 6–2. Receiving tubes are often connected in series. Suppose you have a 6-volt battery. How many 12-type tubes could you use in series if each requires 1.5 volts across its filament?

Problem 7–2. Suppose you were going to use five 199-type tubes in a series filament circuit. How many volts will be necessary?

Problem 8–2. What would be the total resistance of five 199-type tubes in series?

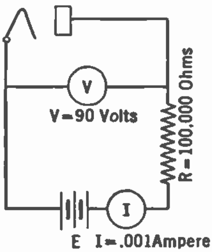


FIG. 20.—A problem in a resistance-coupled amplifier. What is the value of E?

Problem 9–2. The resistance of 199-type tube filaments is about 50 ohms. How much current would flow in Problem 8? Assume $E = 3$.

Problem 10–2. How much resistance would be necessary if one 199-type tube is to be run from a 6-volt storage battery? Two tubes? Five tubes?

Problem 11–2. An incandescent lamp has a resistance, when hot, of about 55 ohms, and requires one ampere to light at full brilliancy. How many could be run in series on a 110-volt circuit?

Problem 12–2. How many volts are required to force one milliampere through a circuit composed of a vacuum tube and a resistance, if the latter has 100,000 ohms and 90 volts are required at the tube? (See Fig. 20.)

25. Characteristics of parallel circuits.—A parallel circuit is represented in Fig. 21. It consists of several branches. The voltage across each branch is the same as that across every other branch and is equal to the voltage of the battery. The total current supplied by the battery is the sum of the currents taken by the branches. The resistance of the group may be found by

$$\frac{1}{R} = \frac{1}{R_1} + \frac{1}{R_2} + \frac{1}{R_3}$$

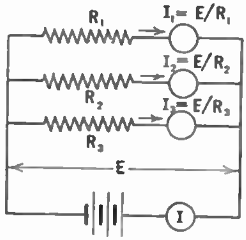


FIG. 21.—A parallel circuit.

where R is the resultant or total resistance, and R_1, R_2, etc., are the individual resistances.

The resultant resistance of several units in parallel is less than the individual resistance of any of the components. If two equal resistances are in parallel, the resultant is one-half the resistance of one. Thus if two 10-ohm resistances are connected in parallel, the resultant resistance is 5 ohms. What would it be if they were connected in series?

If any number of equal resistances are in parallel, the resultant resistance is the individual resistance divided by the number of units.

If only two unequal resistances are in parallel the resultant may be calculated by dividing their product by their sum:

$$R = \frac{R_1 \times R_2}{R_1 + R_2}.$$

Example 3–2. What is the parallel resistance of two units which have resistances of 4 and 5 ohms?

This can be solved by either of the formulas given above.

$$\frac{1}{R} = \frac{1}{4} + \frac{1}{5}$$
$$= .25 + .20$$
$$= .45$$
$$R = 1/.45 = 2.22 \text{ ohms.}$$

Or,

$$R = \frac{R_1 \times R_2}{R_1 + R_2}$$

$$= \frac{4 \times 5}{4 + 5}$$

$$= \frac{20}{9} = 2.22 \text{ ohms.}$$

Example 4–2. Suppose, as in Fig. 22, these two resistances in parallel are placed in series with a resistance of 1 ohm and across a battery of 6 volts. What current would flow out of the battery and through each resistance?

The total resistance is 2.22 + 1 = 3.22 ohms. The current flowing, then, is 6 ÷ 3.22 = 1.86 amperes. This current through the combined resistance of

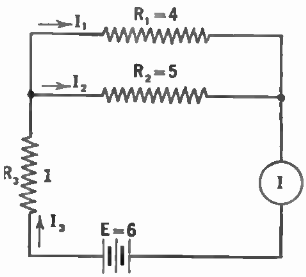


Fig. 22.—Solve for the various currents.

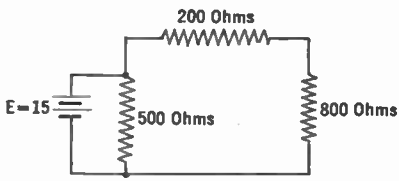


Fig. 23.—What is the voltage drop across the 800 ohms?

the 4- and 5-ohm units produces a voltage drop of $I \times R$ or 1.86 × 2.22 or 4.14 volts. This voltage across 4 ohms produces a current of 4.14 ÷ 4 or 1.035 amperes, and across 5 ohms produces a current of 0.827 ampere. These two currents added together are 1.862 amperes, which checks our calculation above.

Problem 13–2. The usual battery-operated radio receiver has five tubes of the 201-A type, each taking .25 ampere. What is their combined resistance. and how much current do they take from a 6-volt storage battery if an external rheostat is used to cut down the voltage to 5 across the tube? What is the value of this resistance in ohms?

Problem 14–2. A circuit has three branches of 4, 6, and 8 ohms. A current of 4 amperes flows through the 6-ohm branch. What current flows through the other branches?

Problem 15–2. Consider the circuit of Fig. 23. What is the voltage drop across the 800-ohm resistor?

Problem 16–2. In Problem 13 suppose one of the five tubes were a power tube requiring one-half ampere. If it is connected in parallel with the other tubes, what will be the value of resistance needed? Will each tube get its rated voltage under these conditions?

Experiment 2–2. Connect as in Fig. 22 several shunt resistances such as tubes, rheostats, fixed filament resistors, etc., in series with a battery and a rheostat. Measure the parallel resistance and individual resistances by reading the current through them separately and in parallel and the voltage of the battery. Test the relation $\frac{1}{R} = \frac{1}{R_1} + \frac{1}{R_2} + \frac{1}{R_3}$.

26. More complicated circuits.—Some radio circuits are combinations of series and parallel circuits. A common form and its equivalent are shown in Fig. 24. Other more complicated circuits

$$I_1 = \frac{E(R_2+R_3)}{R_1R_2+R_1R_3+R_2R_3}$$

$$I_2 = \frac{ER_3}{R_1R_2+R_1R_3+R_2R_3}$$

$$I_3 = \frac{ER_2}{R_1R_2+R_3R_3+R_2R_3}$$

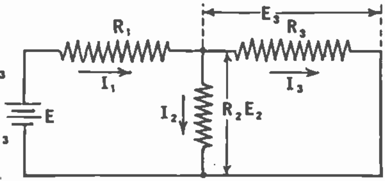


Fig. 24.—A complex circuit and its solution.

may arise in practice and may be solved by more complex algebra than is needed for simple Ohm's law cases. All such circuits can be reduced to more simple circuits by the application of certain rules which may be found in books on complicated networks of resistances, voltages, and current. In "Transmission Circuits for Telephone Communication," by K. S. Johnson, may be found the equivalent circuits of many very complex arrangements of apparatus.

27. Detection and measurement of current.—We cannot see or hear or smell the passage of an electric current through a circuit. It must be made evident to us by its effect upon the circuit. There are three kinds, a magnetic effect, a chemical effect, and a heating effect. Wire gets hot if too much current flows through it; two dissimilar metals (copper and zinc, for example) placed in a solution of one of them (copper sulphate) give off gas bubbles when a wire connects them together externally; a wire carrying an electric current if brought near a compass needle will cause the needle to change from its habitual north-south position.

These are the three fundamental effects of electricity. Any of them can be used to detect the presence of a current or even to measure the rate at which the current flows. A hot wire ammeter (Fig. 25) for example is merely a wire which sags when it gets hot by passing a current through it. A needle is attached to the wire and moves across a scale as the wire gets hot. We might measure the quantity of gas given off per unit of time and thereby deduce the amount of current flowing through an electric "cell."

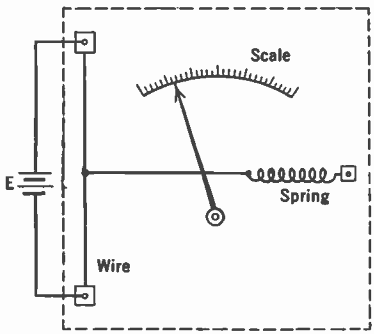


Fig. 25.—Hot wire ammeter.

Most measuring instruments use the magnetic principle. They consist of a permanent magnet near which is a coil of fine wire wound on a movable pointer. Current flowing through this coil makes a magnet of it. It changes its position with respect to the permanent magnet just as a compass needle does when brought near a current carrying wire. Such instruments can be made sensitive enough to measure currents as low as one-millionth of an ampere or to detect the flow of even smaller currents than this.

28. Ammeters.—Meters to measure current are called ammeters. They are connected in series with the source of current and the device into which the current flows. They are made less sensitive—so they will measure large currents—by shunting them by copper wires so that only a small part of the total current flowing actually goes through the meter.

A very simple current-indicating device consists of a coil of wire through which the current flows and a compass placed in the center. A modern highly sensitive meter is a delicate instrument in which the compass needle is replaced by a carefully pivoted coil of wire carrying a pointer. These instruments are shown in Fig. 26.

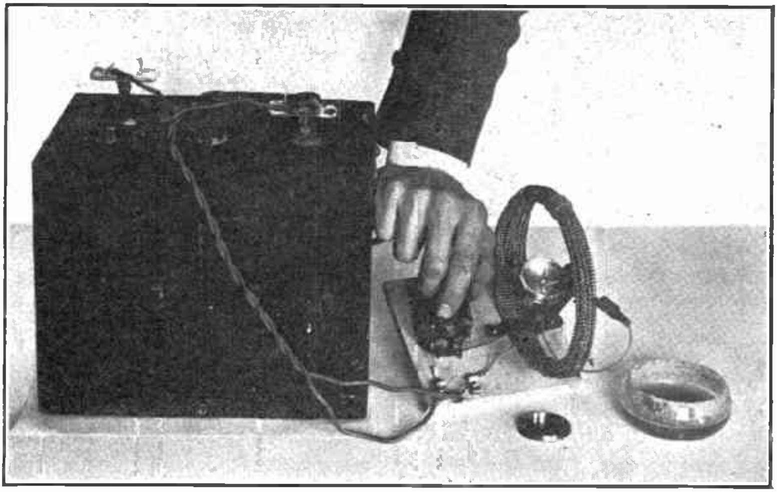


FIG. 26(*a*).—A simple form of galvanometer. When a current flows through the coil of about 25 turns, a magnetic field is created which effects the position of the needle.

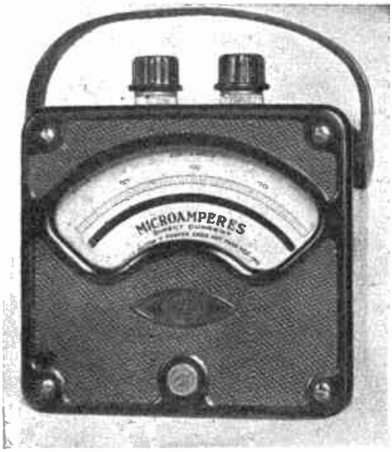


FIG. 26(*b*).—A modern meter (Westinghouse type PX) which reads full scale 200 microamperes and which will indicate a current of less than 2 microamperes.

29. Voltmeters.—Ammeters have low resistance. They are in series with the apparatus taking current from the source, as shown in Fig. 27.

FIG. 27.—Ammeters are connected in series with the resistance into which the current flows

Voltmeters, on the other hand, must read the voltage across some part of the circuit. They must not permit much current to flow because this current would be taken away from the circuit. They have a high resistance. They are really high resistance ammeters. Thus an ammeter, the Jewell 0–1 milliampere meter for example, can be made to read volts by putting it in series with a high resistance and across the circuit to be measured.

For example, 1 volt is required to give 1 milliampere of current through 1000 ohms. Thus if we have a 1.0 milliampere meter and we wish to measure a voltage of the order of 1 volt, we need only a resistance of 1000 ohms. Then the figures on the meter scale will read volts instead of milliamperes. Such a series resistance is called a **multiplier.**

A Weston Model 301 meter reading 1.0 milliampere full scale will measure a maximum current of 50 ma. if a resistance of 0.57 ohm is placed across it. If the resistance is reduced to 0.27 ohm, the meter will read 100 milliamperes when its needle points to 1.0 milliampere. Weston Models 280 and 301 voltmeters have a resistance of about 62 ohms per volt. Thus a meter reading a maximum of 100 volts has a resistance of 6200 ohms.

Problem 17–2. How much current is required for full scale deflection on a Weston Model 301, 50-volt voltmeter?

30. Sensitivity of meters.—A sensitive current-measuring meter is one which will measure very small currents but which has a low resistance. A sensitive voltmeter is one which will give a large needle deflection through a very high resistance. Voltmeters which are used to measure the voltage of high resistance devices such as B eliminators must have high resistance in order that the current taken from the device shall not be great enough to lower appreciably the voltage of the device.

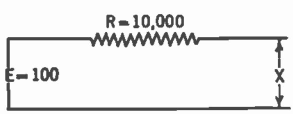


Fig. 28.—A low resistance voltmeter placed at X will not read the open circuit voltage.

Example 5–2. Suppose we are to measure the voltage across the circuit at the point X in Fig. 28. The voltage at X depends upon the current taken by the meter. What is desired is the "open-circuit" or "no-load" voltage across X, that is, the voltage existing there if no current is taken by the meter. If no current flows, there is no voltage drop in the resistance R and hence the voltage at X is the voltage of the battery, or 100 volts. Suppose, however, the meter nas a resistance of 1000 ohms. The current flowing is given by Ohm's law

$$I = E/R$$
$$= 100 \div (10{,}000 + 1000)$$
$$= \frac{100}{11{,}000} = .0091 \text{ ampere or } 9.1 \text{ milliamperes.}$$

This current thrcugh the 10,000-ohm resistance R (which may be the internal resistance of the battery E (Section 49) causes a voltage drop across this resistance of $I \times R = .0091 \times 10{,}000 = 91$ volts.

The voltage actually recorded on the meter, then, is the difference between the battery voltage and the drop across the resistance R, or

$$\text{voltage at } X = E - (I \times R) = 100 - 91 = 9.0 \text{ volts.}$$

If, however, the meter is a high-resistance meter, say 1000 ohms per volt, that is, 100,000 ohms for a meter designed to read 100 volts, the current taken from the battery would be

$$I = E/R = 0.00091 \text{ ampere}$$

and the IR drop across the resistance R would be only

$$E = IR = (0.00091 \times 10{,}000)$$
$$= 9.1 \text{ volts}$$

and the voltage read at X would be 100 − 9.1 volts or 91.9 volts.

In other words the high-resistance voltmeter gives a reading much nearer the open-circuit or no-load voltage desired.

31. Ammeter-voltmeter method of measuring resistance.—The example in the above section gives a clue to a good method of measuring the resistance of a device. The method consists in measuring the voltage across the device when a measured current flows through it. If the resistance of the voltmeter is high compared to that of the device, its own resistance need not be considered, and the inclusion of the ammeter into the circuit need not be taken into account aside from exceptional cases.

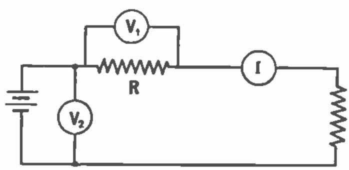


FIG. 29.—Ammeter-voltmeter method of measuring resistance.

Example 6-2. Consider the circuit in Fig. 29. A voltmeter across the device whose resistance is unknown reads 75 volts, and the current meter (I) indicates a current of 0.05 ampere. What is the unknown resistance?

$$R = E/I = 75 \div 0.05 = 1500 \text{ ohms.}$$

32. Voltmeter method of measuring resistance.—If the resistance of a voltmeter is known, a resistance can be measured by its use and a battery. Weston Models 301 and 280 each have resistance of 62 ohms per volt, so that a 50-volt meter would have a resistance of 3100 ohms. Take two readings, one of the battery alone and one of the battery in series with the unknown resistance. Then the desired resistance may be found from

$$R = \left(\frac{E_b}{E} - 1\right)R_m$$

where E_b = Voltage of battery alone;
E = Voltage across battery and resistance;
R_m = Resistance of meter.

33. Use of low-resistance voltmeter and milliammeter in high-resistance circuits.—A high-resistance voltmeter is expensive but is necessary when the voltage output of a socket power device for supplying plate voltages to a radio set, or any other device which has a high resistance, is to be measured. The current taken by the meter is so low that the resistance drop, caused by this current flowing through the internal resistance of the device, is small compared with the voltage being measured.

A method of using a low-resistance voltmeter and a milliammeter is shown in Fig. 30. Suppose the milliammeter is placed in series with the output resistance of the device across which the voltage is to be measured. Suppose the current without the voltmeter attached is I and the current with the voltmeter attached is I'. Let E' be the voltage indicated by the voltmeter when the key is pressed. The resistance in both cases is the ratio of the voltage and current. Thus,

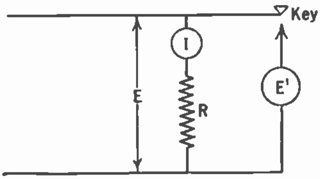


Fig. 30.—A means of avoiding the use of an expensive high resistance voltmeter.

I = current without voltmeter;
E = voltage without voltmeter;
I' = current with voltmeter;
E' = voltage with voltmeter;

$$R = \frac{E}{I} = \frac{E'}{I'},$$

whence E = desired voltage

$$= E' \times \frac{I}{I'}$$

and $$R = \frac{E'}{I'}.$$

34. Resistance measurement.—Resistances are usually measured by what is known as the "comparison" method, that is, by comparing them with resistance units whose values are known. For example, we might measure the current through an unknown resistance, R_1, as in Fig. 31, and then adjust a variable resistance,

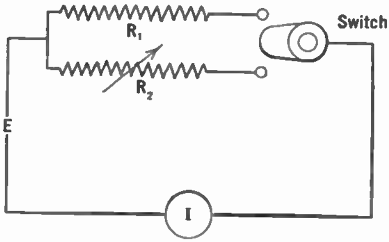


FIG. 31.—Measuring resistance by comparison.

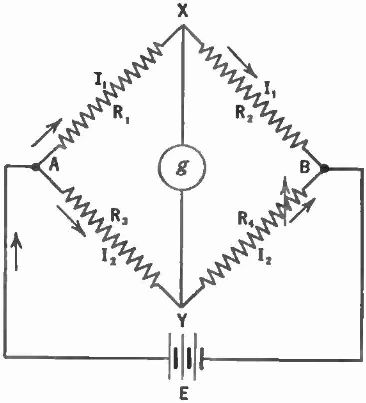


FIG. 32.—Wheatstone bridge for measuring resistance.

R_2, whose values may be read directly until the same current flows under the same e.m.f. The two resistances are then equal in value.

The usual laboratory method employs a Wheatstone bridge. In diagrammatic form it is represented in Fig. 32, in which R_1 and R_2 are fixed resistances whose values are known, R_3 is the unknown resistance whose value is desired, and R_4 is a variable resistance to which the unknown is compared and the values of which are known. The method is as follows. A current is led into the "bridge" arrangement of resistances at the points A and B and a sensitive current indicating meter placed at the points X and Y. The values of R_1, R_2, and R_4 are adjusted until the meter, g, shows that no current flows through it, that is, there is no difference in voltage between the two points X and Y which would force current through the meter. In other words X and Y are at the same voltage.

The total current I divides at A and flows into the " arms " of the bridge forming the currents I_1 through R_1 and R_2 and I_2 through R_3 and R_4. If there is no potential difference between X and Y, the voltage drop along R_1 is equal to the voltage drop along R_3.

Thus $$I_1R_1 = I_2R_3 \tag{1}$$

Similarly $$I_1R_2 = I_2R_4 \tag{2}$$

Dividing (1) by (2) $$\frac{R_1}{R_2} = \frac{R_3}{R_4}. \tag{3}$$

Suppose R_1 and R_2 are equal in value. Then equation (3) becomes

$$1 = R_3/R_4$$

or

$$R_3 = R_4,$$

and to find the value of the unknown resistance R_3 we need only adjust R_4 (whose values are known) until no current flows through the meter. Then the two resistances are equal. Suppose, however, that the unknown resistance is much larger than any value we can obtain by adjusting R_4. For example, let it be ten times as large. Then it is only necessary to make R_1 ten times as large as R_2 when (3) becomes

$$R_1/R_2 = R_3/R_4 = 10$$
$$R_3 = 10\ R_4,$$

and it is only necessary to adjust R_4 until no current flows through the meter and to multiply the resistance of this standard R_4 by 10 to get the value of the unknown resistor R_3.

The resistances R_1 and R_2 are called the ratio arms; R_4, the standard resistance, is usually a resistance " box," that is, a box in which are a series of resistance units accurately measured and equipped with switch arms so that any value of resistance may be

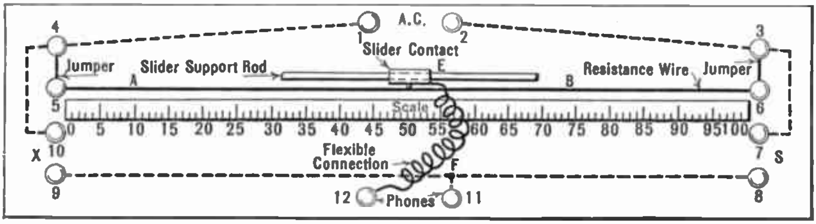


FIG. 33.—A single slide wire bridge.

obtained. A simple " slide wire " bridge is shown in Fig. 33. The unknown and known resistances are compared by means of a slider on a piece of resistance wire. The relative lengths of the wire provide the ratio arms R_1 and R_2.

CHAPTER III

PRODUCTION OF CURRENT

ELECTRICAL energy does not exist in nature in a form useful to man. It must be transformed from some other form of energy. For example, the mechanical energy of a motor, or steam engine, may be transformed into electrical energy by means of a generator.

The commonest sources of current useful to radio workers are the **battery** and the **generator.** The battery is a device which converts chemical energy into electrical energy; the generator uses up mechanical energy with the same result.

35. Batteries.—A **battery** is made up of one or more units called **cells.** The essentials of the cell are three: two conductors called **electrodes,** usually of different materials, and a chemical solution known as the **electrolyte** which acts upon one of the electrodes more than it does upon the other. In this action, one of the electrodes is usually " eaten up," and when this conductor, usually a metal, is gone, the battery is exhausted; it must be thrown away or the metal replaced. If the metal can be replaced by sending a current through the cell from some outside source, that is, by reversing the process through which the cell was exhausted, the cell is known as a **secondary** or **storage** cell. If the cell must be thrown away when one of the electrodes is "eaten up," it is called a **primary** cell. The dry cell is a well-known example.

Experiment 1–3. If a plate of copper and a plate of zinc are placed in dilute sulphuric acid and a sensitive meter is placed across the terminals as shown in Fig. 34, a voltage of definite polarity will be indicated. The positive terminal of the voltmeter must be placed on the copper plate in order that the meter needle shall move in the proper direction. The copper plate is therefore positive; the zinc is negative. If a heavy external wire is attached to the plates, a current flows; the zinc is slowly dissolved, hydrogen bubbles appear at the copper plate, and finally the voltage of the cell falls off. Other combinations of metals should be tried.

The number of combinations of conductors and solutions that will make up a primary cell is very large; only a few of them are useful. Some deliver but small currents and low voltages, others give off noxious fumes, others do not last long enough to be practical.

The e.m.f. of such a cell depends upon the nature of the electrolyte and the materials from which the plates or electrodes are

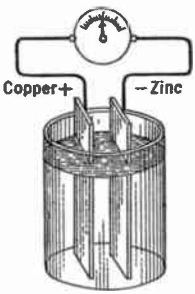


FIG. 34.—A simple primary cell.

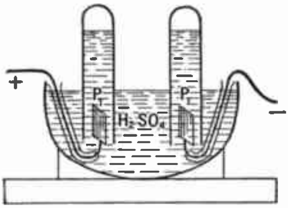


FIG. 35.—An experiment in electrolysis.

made. Copper and zinc plates immersed in a solution of dilute sulphuric acid will give an e.m.f. of about 1 volt regardless of the size of plates or their distance apart. Zinc and carbon plates in chromic acid give an e.m.f. of about 2 volts.

Until the plates are connected externally by a conductor there is a difference of electrical potential existing between the two electrodes but no flow of current. This voltage is known as the e.m.f. of the cell. When the plates are connected and the cell is put to work the destruction of the zinc begins. When the zinc is all destroyed the cell is dead.

36. Electrolysis.—The appearance of hydrogen bubbles at the copper electrode forms the basis of an interesting experiment which is illustrated in Fig. 35.

Experiment 2-3. Dip platinum electrodes into a solution of sulphuric acid and pass a current through them from a battery of about 10 or 12 volts.

Hydrogen will be evolved at the electrode attached to the negative battery terminal and oxygen at the other. These gases will exert sufficient pressure to force the solution out of the inverted test-tubes. If the volumes of the two gases are measured it will be found that the hydrogen always occupies just twice the volume required by the oxygen—which is one of the best proofs we have that water is made of two atoms of hydrogen combined with one of oxygen, whence arises the familiar chemical formula for water, H_2O.

This phenomenon in which a substance is broken down by dissociation and then under the action of an electric current is deposited on one of the electrodes is known as **electrolysis.** In this case if the solution had been copper sulphate, copper would have been deposited on the negative electrode. In the practice of electroplating, metal from one electrode is deposited on another, the strength of the solution, which is a solution of the metal to be deposited, remaining unchanged.

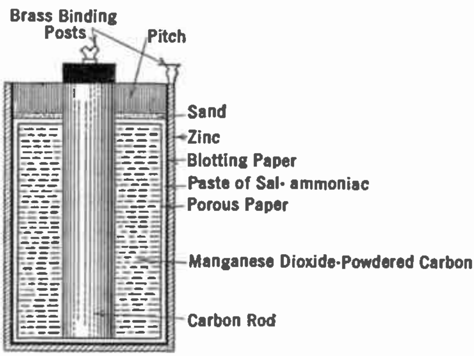


Fig. 36.—Construction of dry cell.

37. Common dry cell.—The common dry cell is illustrated in Fig. 36. The zinc container is the negative electrode, the carbon rod in the center is the positive electrode. The electrolyte is a mixture of powdered carbon and manganese dioxide moistened with a solution of salammoniac. The voltage of the cell as measured by a voltmeter is about 1.5 volts. The ordinary B batteries used in radio are made up of many small 1.5-volt cells connected in series

38. The storage cell.—When the zinc container of the dry cell is eaten up, the cell must be thrown away. In the storage battery neither of the electrodes is eaten away, but the nature of one plate is changed and when a current is sent through the battery from some external source this material is changed back to its original form, so that the cell is said to be "charged" and can be used again.

The storage cell has two electrodes, one of lead and one of lead peroxide immersed in a dilute solution of sulphuric acid. The usual storage battery is made up of three cells in series, producing a voltage of about 6 at the terminals. The positive terminal is usually marked, either with a red terminal, or a large cross, or in some other way. It is important to know the polarity of the battery when charging it. The positive post of the battery should be connected to the positive post of the charging line.

Experiment 3–3. If two lead plates about 6 inches square are immersed in a dilute solution of sulphuric acid—say one part of acid to ten of water—and connected in series with a battery of 6 or 8 volts and an ammeter, a current will be seen to flow, and the color of the plate attached to the positive terminal of the battery begins to change and the evolution of hydrogen bubbles at the other plate will be observed. The current soon decreases. Now replace the external battery with an incandescent lamp or an electric bell and note that current flows out of the lead cell and through the light or the bell.

39. Internal resistance.—One might think that an unlimited current could be secured from a battery if it were short-circuited. Such is not the case. A very low-resistance ammeter placed across a dry cell gives a definite reading—it is not unlimited. Something must be in the circuit which has a resistance greater than that of the ammeter or the connections. For example a new dry cell will deliver about 30 amperes through wires of very low resistance.

This something which restricts the current to a limited value is the **internal resistance** of the cell. This resistance depends upon the construction of the cell, its electrode and electrolyte material, the distance apart of the electrodes, the condition of the cell—whether new or old. The older the cell the smaller the area of electrode in contact with the electrolyte and the greater the resistance. The current delivered by a cell is

$$I = \frac{E}{r + R}$$

when r = internal resistance of cell;
R = external resistance of circuit.

When a dry cell shows but a few amperes on short-circuit, the chances are that its zinc case is badly eaten up. A voltmeter which requires very little current for a deflection will still read normal voltage, 1.5, because the small current through the cell does not cause appreciable voltage drop. The ammeter, however, draws all the current the cell can deliver. This current must flow through the cell as well as through the external circuit and hence there is a large voltage drop within the cell, leaving little voltage to force current through the meter.

Cells which have a large internal resistance deliver but small currents; low-resistance cells deliver large currents.

When one tests a dry cell with an ammeter, he is actually ascertaining the condition of the cell by measuring the internal resistance. When the cell gets old or has been exhausted due to too heavy currents, its internal resistance becomes high and an ammeter reads but small current when placed across it.

The storage cell is a very low-resistance device. Its terminal voltage when fully charged is about 2.1 volts and it has a resistance of about 0.005 ohm. Placing an ammeter across such a cell is dangerous. The meter will probably be ruined.

Example 1–3. A dry cell on short-circuit delivers 30 amperes. Its terminal voltage is 1.5 volts. What is its internal resistance?

By Ohm's law,

$$I = E/r$$

$$30 = 1.5/r$$

$$r = \frac{1.5}{30} = 0.05 \text{ ohm.}$$

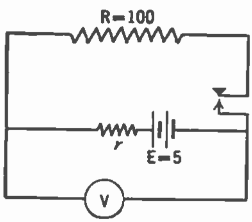


Fig. 37.—A problem in internal resistance.

Example 2–3. The e.m.f. of a battery is 5 volts. When 100 ohms are placed across it the voltage V falls to 4 volts. What is the internal resistance of the battery?

In Fig. 37, $R = 100$ ohms, $r =$ the internal resistance of the battery, the voltage drop across the 100 ohms is 4 volts, which leaves one volt drop in the internal resistance of the cell. The current through the external 100-ohm resistance is, by Ohm's law,

$$I = 4/100 = .04 \text{ ampere.}$$

This current must also flow through the internal resistance of the battery and there it causes a voltage drop of one volt.

$$E = I \times r$$
$$1 = 0.04 \times r$$
$$r = 1/.04 = 25 \text{ ohms.}$$

Note that the internal resistance of the cell is represented as being in series with the voltage and the external resistance. This is because the current must actually flow through the internal resistance of all such voltage generators, and hence the resistance of the device is represented in series with the remainder of the circuit. Care must be taken in such representations not to place the voltmeter in the wrong place. In Fig. 37 the voltmeter is actually placed across the battery and its internal resistance, which is connected directly to the 100-ohm resistance.

The voltage of the cell on open circuit is its **e.m.f.** Under load the voltage falls, and is now labeled as the p.d. (potential difference). The e.m.f. of high-resistance cells can only be measured by high-resistance meters, those that take but little current from the cell. When the voltage of a cell or battery is mentioned its e.m.f. is assumed unless otherwise labeled.

40. Polarization.—In common with all other cells the zinc-copper sulphuric acid cell (Fig. 34) suffers from **polarization.** The hydrogen bubbles which surround the copper plate decrease its surface in contact with the active liquid. This increases the cell's resistance. In addition, a minute voltage is set up between the hydrogen and the copper. This voltage is opposite to the useful voltage and has the same effect upon the usefulness of the battery as an addition to the cell's internal resistance.

Various means are taken to overcome the bad effects of polarization. Chemicals may be placed in the cell to supply oxygen, which will combine with the hydrogen to form water; shaking the cell may remove the hydrogen bubbles and decrease the resistance of the cell. The manganese dioxide used in dry cell construction is a depolarizer. But these are only temporary remedies. Sooner or later the internal resistance of the cell becomes so high that the cell is no longer useful. A dry cell which has had large currents taken from it becomes polarized. If it is allowed to stand for a time, the chemicals put into the cell to do away with the polarization products have the chance to "catch up" and the cell is said to have "recuperated." For this reason dry cells and others which tend to polarize are used only on intermittent service. Where a constant current is required a different type of cell is used.

41. Cells in series.—Cells and batteries may be connected together in several ways. When the positive terminal of one cell is connected to the negative terminal of the next cell, as in Fig. 38, they are said to be connected in **series**. Under these conditions, the voltage appearing at the two ends of the series of cells is the

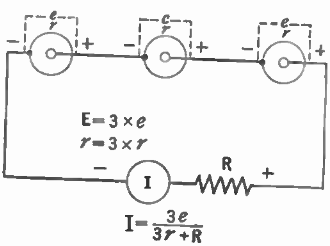


FIG. 38.—Cells in series.

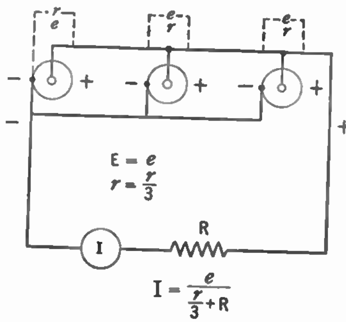


FIG. 39.—Cells in parallel.

sum of the individual cell voltages. For example, if we connect four dry cells in series, each cell having a voltage of 1.5, a voltmeter across the two ends will register 6 volts. At the same time the total internal resistance is the sum of the individual resistances and whatever current flows must flow through this resistance.

If the ends of the battery are connected together with a wire of resistance R the current that will flow may be obtained by Ohm's law as

$$I = \frac{Ne}{Nr + R}.$$

42. Cells in parallel.—When the positive terminal of one cell connects to the positive terminal of the next cell, and the negative terminals are connected together, as in Fig. 39, the cells are said to be connected in **parallel.** Under these conditions the terminal voltage of the combination is the same as the terminal voltage of each cell, but the internal resistance has been divided by the number of cells, N, and has become r/N.

If the ends of the battery are connected together with a wire whose resistance is R, the current that will flow is

$$I = \frac{e}{\frac{r}{N} + R}.$$

Cells may also be connected in what is called a **series-parallel** arrangement. In Fig. 40 are P sets of S cells in series, and the sets themselves are connected in parallel.

If the battery of cells shown in Fig. 40 is connected to a wire whose resistance is R, the current that will flow is

$$I = \frac{Ne}{RP + Sr},$$

where $N = P \times S$.

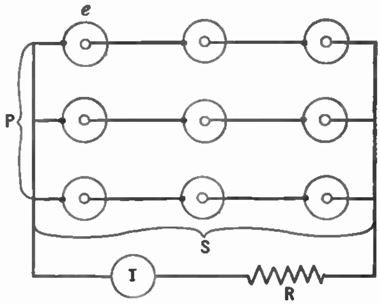


FIG. 40.—Cells in series-parallel.

43. Magnetism.—The second common source of electric currents is the generator. The magnet is the heart of the generator.

Magnets obey the same laws as the fundamental electrical charges mentioned in Section 3 in Chapter I. *Like magnetic poles repel each other, unlike poles attract.* Two magnets will repel each other if their North poles are turned toward each other, but will attract each other with considerable force when a North and a South pole are brought near.

44. Oersted's experiment.—A Danish experimenter, Oersted, in 1819 made the first of a series of discoveries concerning the relation between electricity and magnetism which resulted in many modern applications of electricity. His experiment can be repeated by anyone who has a compass, a battery, and a wire.

Oersted's experiment demonstrated that a conductor carrying a current of electricity affects a compass needle just as a bar magnet does. Another experiment will teach us more about this important phenomenon known as *electromagnetism.*

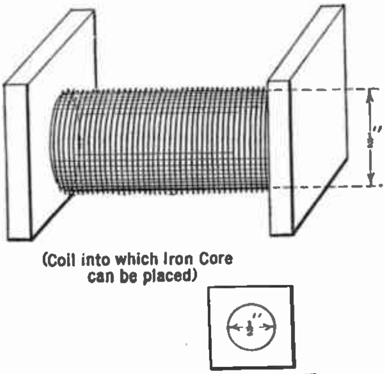


FIG. 41.—A solenoid.

Experiment 4–3. Wind up about 1000 turns of rather fine wire, say No. 28 d.c.c., on a form about a half-inch in diameter or with a hole large enough that a bar magnet can be put in it easily, similar to that illustrated in Fig. 41. Connect it in series with a battery of about 6 volts, and bring a compass near its two ends. Reverse the current through the coil, and note change in direction of the compass needle motion. Note that the two ends of the coil act toward the compass needle just as a bar magnet would. Determine which of the coil ends is North and which is South by comparing their action on the compass with the action produced by the bar magnet whose poles are marked or by the position the needle takes with respect to the earth's poles.

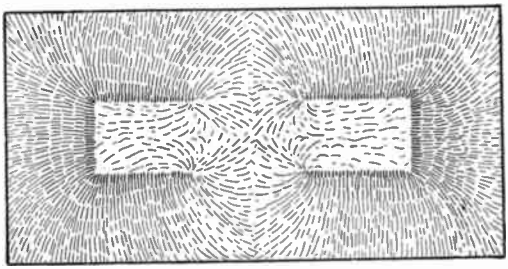


FIG. 42.—How the lines of force about a bar magnet are located.

Experiment 5–3. Scatter a quantity of fine iron filings on a piece of cardboard about a foot square. Place one end of a bar magnet under the cardboard, and tap the board until the filings assume a fixed position. Repeat using the other end of the bar magnet, and then with a horseshoe magnet, and finally with the coil of wire through which a current is flowing. Place the bar magnet parallel to the cardboard and again scatter iron filings. Repeat with the coil magnet. Place the bar magnet inside the coil and remove from the cardboard to such a distance that, with no current flowing in the coil, the iron filings are affected but little. Connect the battery to the coil and note the increase in action among the iron filings. Repeat with battery connected and cardboard removed to such a distance that the filings are not affected. Then put the bar magnet inside the coil and note increased effect.

Such experiments demonstrate that coils carrying electric currents have much the same properties as iron bars which have been magnetized. The fact that such a coil or a magnet affects iron filings or compass needles even though some distance separates them, shows that in the space between them exists some force. The iron filings show the general distribution of this force. They tend to arrange themselves along lines which concentrate in strength at the two ends. These lines are called **magnetic lines of force.** The concentration points are called the **poles.** The space through which the lines pass is called the **magnetic field.**

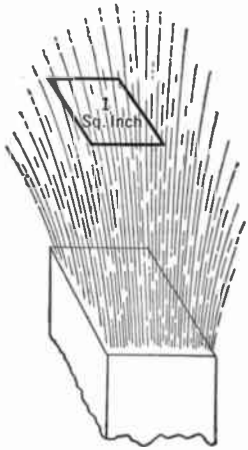


Fig. 43.—The number of lines of force going through one square inch or other unit of area is known as the flux density.

The number of lines per unit of area, as in Fig. 43, is called the **field intensity** or **flux density**; and when one line goes through 1 sq. cm. the field strength is one Gauss. The total number of lines through any given area is called the **flux**, and to find the flux it is only necessary to multiply the field strength, H, by the area. Thus

$$\text{flux } \theta = A \times H.$$

Magnetic lines of force may be set up in iron much more easily than in air. The ratio of the number of lines, under the action of a given magnetizing force, that exist in iron to those that would exist in air is called the **permeability** of the iron. If one line flows through 1 sq. cm. of air and one thousand through the same area of iron the permeability of the iron is 1000.

The field strength varies inversely as the square of the distance away from the pole as shown in Fig. 43. The nearer the square gets to the pole piece the greater the number of lines. As a matter of fact, halving the distance multiplies the number of lines by four.

The same magnetizing effect can be produced by a strong current acting through a few turns of wire as by a weak current through many turns of wire. If the product of turns and amperes, called the **ampere turns**, is the same in two cases the magnetizing effect will be the same.

It is because of the increased permeability, and of the consequent increase in flux density, that adding the iron core to the solenoid, or coil of wire in Experiment 5–3, is so effective. Soft iron is most easily magnetized, but loses its magnetism with the same rapidity. Permanent magnets are made from steel.

45. Faraday's discovery.—The second important discovery on the way toward present-day electrical machinery was that of the celebrated English experimenter, Faraday. The experiment may be repeated by anyone who has a coil of wire, a bar magnet, and a sensitive current indicator such as the galvanometer used in Experiment 6–3.

Experiment 6–3. Construct a galvanometer like that in Fig. 26*a* and connect to the coil used in Experiment 4–3. Thrust a bar magnet into the coil quickly, and then remove it. Note the motions of the compass needle. Wind up another coil with about the same number of turns but of such a diameter that it can be placed around the first coil easily. Connect the second coil to a battery in series with a 30-ohm rheostat and place over the first coil and then remove with a quick motion. Note the compass needle variations.

In all of the above procedure, note the relation between the compass needle movements and the rapidity with which the various changes are carried out.

Such was Faraday's experiment. When the bar magnet, or the coil carrying a current, was motionless, there was no motion of the needle. When a bar was thrust into the coil the needle moved in one direction, and when the motion of the bar was reversed the needle reversed its motion too. There was no metallic connection between the two coils, or between the coil and the bar magnet—and yet changing the position of one with respect to the other, or changing the direction of magnitude or current through one coil produced some electrical effect in the other circuit.

The facts underlying Faraday's experiment are these: An electric voltage was generated or **induced** in the coil when the bar magnet was thrust into it. A voltage of opposite polarity was generated when the magnet was removed. This voltage sent a current through the coil and the galvanometer so that the needle moved. The same explanation holds when two coils are used, one of them carrying a current, taking the place of the iron bar. Whenever lines of force are cut by a conductor, a voltage is generated in that conductor. So long as the conductor moves so that it *cuts* the lines, that is, does not move parallel with them, a voltage is set up. The more lines per second and the more nearly it cuts the lines at right angles, the greater the voltage. In Fig. 44, so long as the conductor AB moves in the direction of the arrow, no voltage is generated because its motion is parallel to the lines of force. But if AB moves up or down or in a direction through the paper, a voltage will be measured across its terminals.

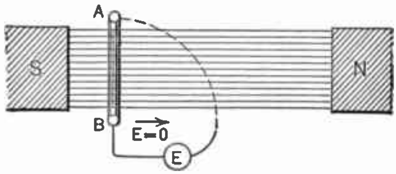


FIG. 44.—So long as the conductor AB moves across the page, no voltage is generated. If it moves perpendicular to the paper, or up and down, a voltage is generated.

This phenomenon is known as **electromagnetic induction,** and voltages and current in the conductor are called **induced,** and the electrical circuit in which they flow is usually called the **secondary,** the inducing circuit is known as the **primary.**

There is no discovery in electrical science which has been so important. Almost every application of electricity to modern life depends upon this discovery of Michael Faraday.

46. The electric generator.—The essentials of a **generator** of electricity are first, a conductor, secondly an electric field, and third a motion of one relative to the other.

A generator converts mechanical energy into electrical energy. Figure 45 is a simple generator. It consists of a turn of wire which is mechanically rotated between two magnets. Remembering that no current due to the induced voltage flows when the conductor moves parallel with the lines of force, and that the maximum voltage is induced when the conductor moves perpendicular to the lines of force, because at this point the maximum rate of cutting takes place, let us see what happens as we rotate the coil.

In position (*a*), Fig. 45, the conductor is moving parallel with the field. No voltage is being generated. As the coil moves, however, it begins to cut the lines at a greater and greater angle until finally at (*b*) it is moving perpendicular to the lines and the voltage is a maximum. Now as the coil continues to move, the part *A*-*B* instead of moving upward across the lines of force moves downward across them. The induced voltage then has reversed its polarity and is increasing toward another maximum position, after which it returns to its original position, where the induced voltage is again zero.

In one complete revolution of the conductor there are two positions at which there is no induced voltage and hence no current in

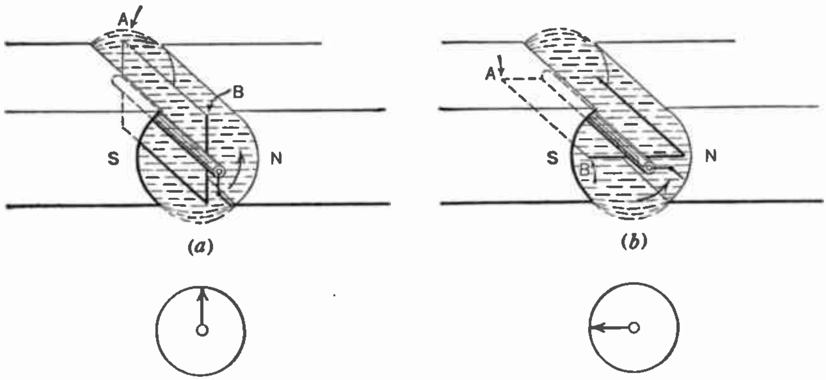


Fig. 45.—In (*a*) the conductor *AB* is moving parallel or along the lines of force. In (*b*) the conductor is moving across or at right angles to the lines. At (*a*) the generated voltage is zero; at (*b*) it is a maximum.

the external circuit, and two in which the voltage is at maximum, although in opposite directions. At intermediate positions, the voltage has an intermediate value.

A complete circle, like a compass, may be divided into 360 degrees. Since the rotating coil moves in a circle, we can label the positions of the conductor in degrees of rotation instead of positions (*a*), (*b*), etc. At the beginning, (*a*), it is at 0 degrees—it has not started to move. Then at (*b*) it is at right angles to its original position (*a*), or it has gone through one-fourth of a complete revolution. It has therefore passed through one-fourth of 360 degrees or 90 degrees. When it is again parallel with the lines of force, it has passed through 180, and when it has gone through three-fourths of 360, or 270 degrees, the voltage is a maximum but in an opposite direction, and finally when it reaches its original position it has passed through a complete circle or 360 degrees.

Let us plot the current induced in the circuit against the degrees through which the coil has passed. Such a plot is shown in Fig. 46. When the current is flowing in one direction we call it positive, when it reverses we call it negative. If the conductor moves at a uniform rate, say one revolution in 360 seconds, we can plot the current induced against time in seconds.

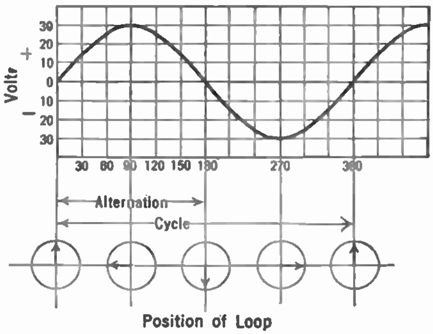


FIG. 46.—Each position of the conductor as indicated by the arrows corresponds to some voltage as shown on the graph—called a "sine wave" of voltage.

One complete revolution is called a **cycle.** The number of cycles per second is known as the **frequency** of the induced voltage. The time required for one complete revolution is called the **period.** One-half cycle, or the part of the cycle during which the voltage is in the same direction, is called **an alternation.**

Such is the current produced by an **alternating-current,** or a.-c., generator. It flows first in one direction, then in another. The generator, of course, is a much more complex machine than we have illustrated here. The magnet is replaced by a heavy iron core covered with wire in which a direct current flows. This produces a strong unidirectional magnetic field. The moving coil is also wound on an iron form and consists of many turns of wire wound in slots.

47. Work done by alternating current.—Some may wonder whether or not a current that is continually reversing its direction—never getting anywhere, so to speak—is useful. It is.

Consider a paddle wheel in a stream of water. To the paddle wheel are attached mill stones. Grain is to be ground between the stones. It matters little whether the water flows continuously turning the millstones in a certain direction, or whether the water flows first one way and then another. So long as the millstones turn against each other, grain will be ground. Work will be done.

The alternating current used to light our homes is usually of 60 cycles, or 120 alternations per second. In some communities 25-cycle current is supplied. In radio installations for use on shipboard, generators usually produce 500-cycle currents. At the high-power radio stations of the Radio Corporation of America at Radio Central, Long Island, are huge alternators which turn out radio frequencies of 20,000 cycles a second. Smaller generators which produce frequencies as high as 100,000 per second have been built but are not in common use.

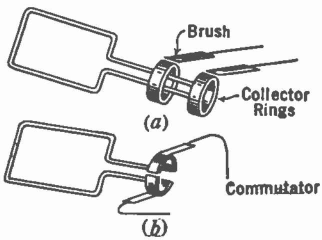


FIG. 47.—Current is taken from an alternating current generator by collector rings; a commutator serves the same purpose on a direct current machine.

48. D.-c. generator.—Current is taken out of a generator by **collector rings.** They are illustrated in Fig. 47. If current flowing in a continuous direction is desired, the collector rings are not used, but instead is used a device called a **commutator.** It is a switch, or valve, which keeps the output current flowing in the same direction by reversing at the proper time the position of the wire with respect to the rotating wire. In this manner the current flows through the external circuit in a single direction, although the current in the conductor which cuts the lines of force must reverse each time the conductor passes through 90 degrees and reverses its direction with respect to the field.

The commutator serves the same purpose as a valve in a pump which keeps water flowing upward whether the pump handle is worked down or up. A machine which sends out current which flows in a given direction is called a **direct-current** generator, and naturally, the current is known as direct current, or d.c.

49. Internal resistance.—The generator too has an internal resistance so that the voltage measured at its terminals differs when different currents are taken from it. The voltage measured across the terminals on a meter requiring little current is called the **open-circuit voltage.** As the current taken from the generator increases, this voltage drops.

50. Electrical power.—Throughout the previous discussion we have spoken of electrical energy in a rather loose way. What do we mean by energy? What is power? What is their relation to work?

Energy is the *ability to do work.* A body may have one of two kinds of mechanical energy, either **potential energy** or **kinetic energy.** The former is due to the position of the body, the latter is due to its motion. A heavy ball on top a flag pole has potential energy because if it falls it can do work, useful or not. It may heat the ground where it falls, or it may be used to drive a post into the ground. A cannon ball speeding through the air has energy because it can do work, useful or otherwise, if it is stopped suddenly. The target may be heated thereby, converting the kinetic energy possessed by the ball into heat energy. The amount of damage done gives the eye a certain measure by which to judge the energy originally possessed by the cannon ball. This energy was originally possessed by the powder and was imparted to the ball when it exploded.

The **power** required to force a certain current of electricity through a wire at a voltage of E volts is the product of the voltage and the current. Thus

Power in watts equals current in amperes times volts,

or

$$P = I \times E.$$

A horsepower is 33,000 foot-pounds per minute. It is equal to 746 watts.

All expressions for power involve the factor of time. In other words, power is the *rate of doing work.* It requires more power to accomplish a certain amount of work in a short time than in a longer time. For example a ton of material raised a foot in the air represents 2000 foot-pounds of work. If it is accomplished by a crane in 1 second of time it represents an expenditure of 2000 × 60 or 120,000 foot-pounds per minute of power. Since one horsepower is equal to 33,000 foot-pounds per minute, the crane has a power of 120,000 ÷ 33,000 or about 3.65 horsepower.

Now if a man raises the ton of material one foot in the air in an hour's time by going up a very long and gradual incline, his power is 2000 ÷ 60 or 33.2 foot-pounds per minute, or roughly one-thousandth horsepower (0.001 hp.). The amount of work done in the two cases is the same—the ton of material has been raised one foot in the air. The *rate of doing work* has changed.

Example 3–3. A generator is rated at 5 kilowatts (5000 watts) output. How many amperes can it supply if its voltage is 110 and it has no appreciable resistance? How many horsepower is this?

Power equals $E \times I$

$$5000 = 110 \times I$$

$$I = 5000/110 = 45.6 \text{ amperes.}$$

Horsepower equals 746 watts.

$$5000/746 = 6.7 \text{ horsepower.}$$

51. Power lost in resistance.—According to the law called the Conservation of Energy, energy can neither be created nor destroyed. It comes from somewhere and goes somewhere. Similarly, all *power*, which is the rate at which energy is used, must be accounted for. The energy required to force current through a resistance must do some work. It cannot disappear. This work results in heating the resistance. Whenever current flows through a resistance, heat is generated and the greater the current the greater the heat. As a matter of fact the heat is proportional to the square of the current. If the wire is heated faster than the heat can be dissipated in heating the surrounding air, the wire melts. Energy has been supplied to the unit at too great a rate.

A resistor used in a power supply device is rated at so-many ohms and as capable of dissipating so-many watts. Thus a 1000-ohm, 20-watt resistor, means that the resistance of the unit is 1000 ohms, and that 20 watts of electrical power can be put into it without danger of burn-out.

Problem 1–3. Electric power is bought at the rate of so-much per kilowatt-hour. Suppose your rate is 10 cents per kilowatt-hour. How much does it cost to run a flat-iron on a 110-volt circuit if it consumes 6 amperes?

Problem 2–3. Assuming that 20 milliamperes direct current flow through the winding of a loud speaker which has a d.-c. resistance of 1000 ohms, what amount of heat in watts (I^2R) must be dissipated? What supplies this power? Suppose an output device is used which has a resistance of only 200 ohms. How much power is saved? Is there any other advantage of the latter arrangement you can see?

52. Expressions for power.—Just as there are three ways of stating Ohm's law, so there are three ways of stating the relation between power, volts, amperes, ohms. Thus:

$$(1)\ P = I \times E \qquad (2)\ P = I^2 \times R \qquad (3)\ P = E^2 \div R$$

Example 4–3. A power supply device supplies 180 volts to a power tube of the 171 type which consumes 20 milliamperes. How much power is taken from the device? What is the resistance of the tube?

The power supplied is $E \times I = 180 \times 0.02 = 3.6$ watts. The resistance into which this power is fed is equal to $P \div I^2 = 3.6 \div .0004 = 9000$ ohms or $E^2 \div P = 180^2 \div 3.6 = 32{,}400 \div 3.6 = 9000$ ohms.

The maximum current that can pass through one's body without serious results is 0.01 ampere. The resistance varies with one's health and the surface in contact, etc. If the finger tips of the two hands are dry, the resistance from one hand to the other is about 50,000 ohms, and thus by Ohm's law the maximum voltage that can be safely touched is 500.

Problem 3–3. Assuming that a man can touch with his dry finger tips a 500-volt street car conductor, and that the resistance of his body is 50,000 ohms, how much power is used up in heating the body?

Problem 4–3. A voltage of 110 is to be placed across a circuit whose resistance must be such that 220 watts can be delivered. What is the resistance of the circuit?

Problem 5–3. How much power is taken from a storage battery of 6 volts which supplies five quarter-ampere receiving tubes?

Problem 6–3. One milliampere of plate current flows through a 100,000-ohm resistor. How much power in heat must the resistor be capable of dissipating?

Problem 7–3. How much current can be sent through a 1000-ohm 20-watt resistor without danger of burning it up? What voltage is required?

Problem 8–3. In a plate voltage supply device the voltage-divider has a total resistance of 5000 ohms. The receiver requires a maximum current of 30 milliamperes. What must be the wattage rating of the resistor?

Problem 9–3. A voltage divider has 220 volts across it and a current of 40 milliamperes flows. What is the wattage rating of the resistor? What is its resistance?

53. Efficiency.—Efficiency is a term that is loosely employed by nearly everybody. Anything which works is said to be efficient, and one's efficiency is often confused with his energy—his ability to do work whether the work is actually carried out or not. The term, however, has a very exact meaning when one uses it in speaking of machines or mechanical or electrical systems of any kind.

Let us consider a steam engine connected to a dynamo, a combination of machines for transforming mechanical energy into electrical energy. If the steam engine consumes one horsepower (746 watts) and delivers 500 watts of electrical energy, it is said to be more efficient than if it delivered only 250 watts. Let us consider two men, one of whom gets a lot of work done in a small amount of time and with an expenditure of little effort. The other gets the same amount of work done but with great effort, perhaps flurrying about from one thing to another instead of tackling his problem in a straightforward manner. The first man is more efficient. He *wastes* less time and energy.

Efficiency, then, is the ratio between useful work or energy or effect got out of a machine to the total energy or power or effort put into it. It is expressed in percentage. A machine that is 100 per cent efficient has no losses; there is no friction in its bearings, or, if it is an electrical device, no resistance in its wires. There are no such machines in use to-day. Efficiency is the ratio of useful power one gets out of a device to the power put into it.

$$\text{Efficiency} = \frac{\text{useful output}}{\text{input}} = \frac{\text{useful output}}{\text{output plus losses}}.$$

Problem 10–3. A generator transmits the greatest amount of power to a load when the internal resistance of the generator is equal to the resistance of the load. Assume any resistance and current and calculate the efficiency of the system. Answer—50 per cent.

Problem 11–3. Seventy-five per cent of the ampere-hours put into a battery are returned by it on discharge. How many hours must a 100-ampere-hour battery be charged at a one-ampere rate?

CHAPTER IV

INDUCTANCE

THE experiments of Ohm, Oersted, and Faraday laid the foundation of modern electrical science. The experiments of the last chapter gave us some idea of what these investigators discovered, and gave us a background for the following fundamental facts.

54. Coupled circuits.—Consider the two coils *P* and *S* in Fig. 48. They are said to be " coupled " when lines of force from one go through the other. When *P* is attached to a battery and the switch closed there is a momentary indication of the needle across *S*. When the switch is opened the needle moves again but in the opposite direction. So long as the current in the primary *P* is steady in value and direction, there is no movement of the needle across the secondary or coils. If a galvanometer is put across the secondary of an ordinary high-ratio audio transformer, and a battery is connected across the primary, the needle of the galvanometer will kick one way when the connection is made, and in the opposite direction when the battery connection is broken. This deflection of the needle indicates a

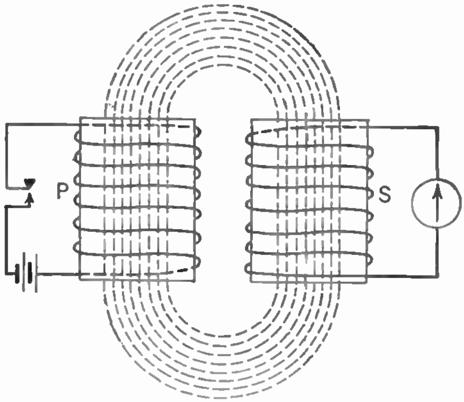


FIG. 48.—If the coils *P* and *S* are coupled so that lines of force from *P* go through *S*, a current indicator will show a flow of current in *S* when the key in *P* is closed or opened.

momentary flow of current in the secondary coil; this current flows only when the primary current is changing, i.e., starting or stopping, not when the primary current is fixed in value or direction.

55. Lenz's law.—There are two fundamental facts about this phenomenon of coupled circuits. The first is that when lines of force couple two coils together, and some change in these lines takes place, perhaps due to a change in the current in the circuit that is producing the lines, a voltage is " induced " in the second circuit. The second fundamental fact is known as **Lenz's law**: this induced voltage is in such a direction that it opposes the change in current that produced it.

Thus when the battery is attached to *P*, lines of force thread their way across the turns of wire in *S*. This movement of the lines of force through *S* induces a voltage across this coil and a current flows in the coil and the apparatus connected to it. This current in the second coil is in such a direction that its field, that is, its lines of force threading through the primary, induces a counter voltage in the primary opposite in direction to the battery voltage across it.

When the battery voltage is broken, the lines of force from the primary current collapse back on the coil, and, in crossing the secondary turns in an opposite direction to that taken when the current in the primary is increasing, induce a voltage in the secondary in such a direction that it tends to keep the primary current flowing.

The result is that it takes a longer time to build up the primary current to its final value at " make " and a longer time for the current to fall to zero at " break."

This phenomenon of induced current is of most fundamental importance. It is the basis of all our modern electrical machinery. Our motors, our dynamos, our radio signals all are the result of our ability to produce changes in one circuit by doing something to another although the two circuits have no metallic connection whatever.

The fact that current takes longer to reach its final value in a circuit in which there is a coil of wire indicates that something about this coil tends to prevent any change in the current. If the current is zero, this property of the coil tends to prevent any current from flowing. If the current already exists, this coil property tends to prevent either an increase or decrease in this value of current.

56. Inertia—inductance.—The property of an electrical circuit which tends to prevent any change in the current flowing is called its **inductance.** It has a mechanical analogue in **inertia.** A flywheel requires considerable force to get up to speed; and after it is started it will continue to run for some time after the driving force is removed. It does not stop suddenly. As a matter of fact it requires considerable force to stop it, and the more suddenly one wants to stop it, the more force he must apply.

Inertia is evident in a mechanical system only when some change in motion is attempted. It is not the same as friction, which is always present.

Inductance is a property of an electrical system in which changing currents are present. It is not to be confused with resistance, which is always present. Current flowing in a resistance circuit stops when the driving force (voltage) is removed. If inductance is added to the circuit, the resistance remaining the same, a longer time will be required for the current to reach its final value, zero, when the voltage is removed.

57. Self-inductance.—Inductance is added to a circuit by winding up a wire into a compact coil. If, for example, 1000 feet of No. 20 copper wire is strung up on poles, it will have a resistance of about 10 ohms and the current into it would reach a final value very soon after a battery were applied. If, however, the wire were wound up on a spool with an iron core, the time required for the current to reach its final value would look like the curve in Fig. 49. Its resistance has not changed; we have merely added inductance.

When the switch is opened a fat spark occurs; this is not true when the wire is strung up on poles. The current seems to try to bridge the gap; to keep on flowing. It does not "want" to stop. This is because of the inductance of the coil.

A single coil can have inductance and can have a voltage induced across it just as though it were the secondary coil shown at S in Fig. 48.

When the current starts to go through the coil, lines of force begin to thread their way out through the coil, thereby cutting adjacent turns of wire, and according to Lenz's law inducing in each turn a voltage in such a direction that it tends to oppose the building up of the current from the battery. When the battery connection is broken, these lines of force fall back upon the coil and

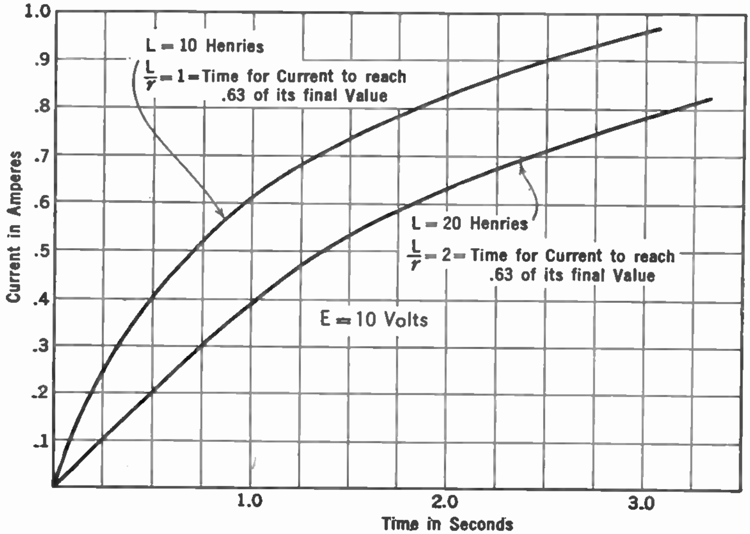


FIG. 49.—Current in an inductive circuit does not rise instantaneously to its maximum value as these curves show.

when cutting the individual turns of wire in the opposite direction they induce voltages in them which tend to keep the battery current flowing.

58. Magnitude of inductance and induced voltage.—The greater the number of turns of wire in a small space, or the better the **permeability** of the core on which the wire is wound, the greater will be the inductance of the coil and the longer time required for the current to reach its final value. The permeability of air is 1.0; that of iron may be as high as 25,000. This means that the inductance of a given coil may be increased 25,000 times by winding it on a core of high permeability iron or alloy such as permalloy in which the permeability may get as high as 100,000. It is composed of nickel and iron.

The induced voltage across such a coil depends upon the rate at which the current is changing and the inductance of the coil. Since the current tends to keep on flowing when an inductive circuit is broken the voltage across the coil must be in the same direction as the battery voltage. Thus if a coil has 100 volts from a battery across it, and the current is suddenly broken, the voltage at the instant of break across the coil will be 100 plus the additional induced voltage. Breaking the current into a highly inductive circuit may set up a tremendous voltage across the coil and a severe shock can be felt by holding the ends of the wire at the moment of break. This is a practical demonstration of Lenz's law.

Example 1-4. In Fig. 50 is an inductance across which is placed a flash lamp and a battery. The current is regulated so that insufficient current goes through the lamp to light it up. Now when the switch is opened the lamp will suddenly light (and may burn out) because of the added voltage across it.

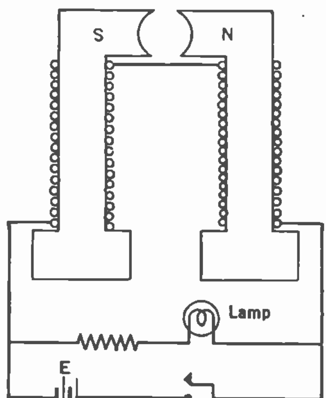


FIG. 50.—An example of Lenz's law. The lamp will light when the key is opened even though insufficient current flows through it when the key is closed.

The inductance of a coil depends upon the number of turns, the manner in which the wire is wound, and the material on which it is wound. If the coil is wound on iron, the inductance will be greater because the lines of force will be concentrated into a smaller space; more lines per unit area will go through a given area of coil.

In radio circuits the coils are invariably wound on non-magnetic cores. In audio circuits iron is utilized to built up large inductances in small spaces and with a minimum of copper wire.

If an a.-c. voltage is placed across a coil, the current through the coil is much less than if a d.-c. voltage were placed across it. This is because of the counter or back voltage induced across the coil by the effects just described. The result is that a seeming decrease in voltage across the coil has taken place, although a voltmeter would indicate that the line voltage was across the coil.

59. The unit of inductance.—When a current change of one ampere per second produces an induced voltage of one volt, the inductance is said to be one **henry**, named from Joseph Henry, an American experimenter who discovered the phenomenon of electromagnetism at the same time as Michael Faraday. Coils added to circuits for the purpose of increasing the inductance of the circuit are properly called "inductors." In this text the words inductance and inductor are used synonymously—incorrectly, probably.

60. Typical inductances.—The coils used in radio apparatus vary from inductances of the order of microhenries to very large ones having over 100 henries in inductance. Broadcast frequency tuning coils are of the order of 300 microhenries, and may be from 1 to 3 inches in diameter wound with from No. 30 to No. 20 wire of from 50 to 100 turns or so. There are a number of complicated formulas by which one can calculate the inductance of coils of various forms and sizes. The ones in Fig. 51 are accurate enough for practical purposes.

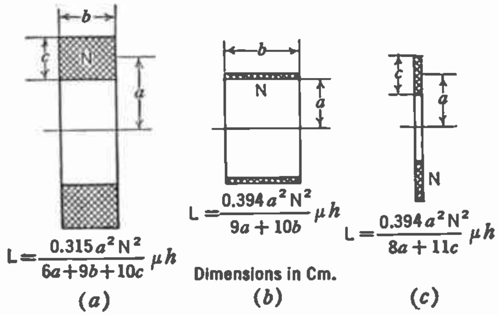


FIG. 51.—Some typical inductances.

These formulas show that the inductance increases as the square of the number of turns. Thus if a coil of 3 units inductance has its number of turns doubled, the inductance will have increased four times or to 12 units. This is true provided there is good "coupling" between turns; that is, if the coil is on an iron core this rule is strictly true, but if the coil is wound on a core of air the rule is only approximately true. It becomes more nearly a fact the closer together the turns of wire.

Problem 1–4. A coil like that in Fig. 51*a* is called a **multilayer** coil. Such a coil is wound to have 1000 turns, in a slot 1 inch square. The distance from the center of the coil to the center of the winding (*a* in Fig. 51) is 2 inches. What is the inductance of the coil in microhenries? Remember that the dimensions given in Fig. 51 are in centimeters and that one inch equals 2.54 cm.

Problem 2–4. A coil like that in Fig. 51*b* is called a **solenoid**. It is the type of coil most often used in radio circuits. The most efficient coil—with the most inductance for the least resistance—is a coil whose dimensions *a* and *b* are equal. Calculate the inductance of such a coil composed of 60 turns of wire in a space of 3 inches, the diameter of the coil form being 3 inches.

61. Coupling.—The closer together the two coils, P and S, Fig. 48, the greater the number of the lines of force due to the primary current that links with the turns of the secondary, and the better the " coupling " is said to be. The better the permeability of the medium in which the lines go, the better the coupling.

The voltage across the secondary of such a two-coil circuit as that shown in Fig. 48 depends upon the sizes of both coils, their proximity, the permeability of the medium, and the rate at which the primary current changes. All of the factors except the rate of change of the primary current are grouped together and called the **mutual inductance** of the circuit.

The secondary voltage, then, is equal to

$$M \times \text{rate of change of primary current,}$$

where M is the mutual inductance and is rated in **henries.**

62. Magnitude of mutual inductance.—Formulas in Fig. 51 show that the inductance of a coil depends upon the square of the number of turns. Doubling the turns increases the inductance four times. Consider two coils built alike and having the same inductance. If they are connected together the total inductance will be equal to that of a single coil of double the turns. In other words the total inductance of two coils connected " series aiding " will be four times the inductance of a single coil. If the connections to one coil are reversed, the total inductance will be zero because the lines of force from one coil will encounter the lines of force from the other coil which are in the opposite direction. The coils are now connected " series opposing."

Consider the series-aiding case, Fig. 52*a*. The total inductance is made up of the inductance of coil 1, that of coil 2, the mutual inductance due to the lines of force from coil 1 which go through coil 2 and the mutual inductance associated with the lines from coil 2 which go through coil 1; these two inductances are equal because the coils are identical.

$$\text{Thus,} \quad L_a = L_1 + L_2 + 2\,M$$
$$= 2\,L_1 + 2\,M \quad (\text{because } L_1 = L_2)$$
$$= 4\,L_1 \quad (\text{by experiment or measurement})$$

$$\text{whence} \quad M = L_1.$$

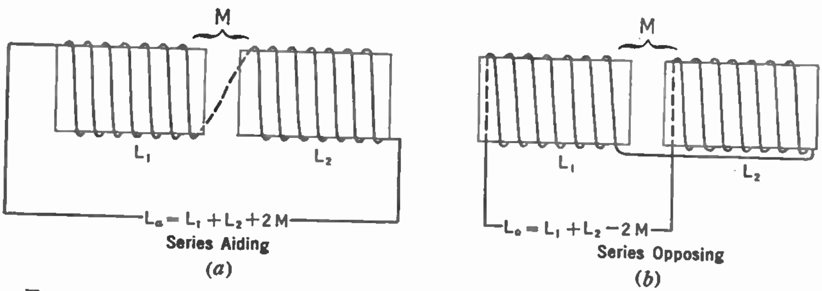


FIG. 52.—Coils may be connected so that their fields aid or "buck" and hence so that the total inductance is increased or decreased.

Now if the coupling in both these cases is less than perfect, if some of the lines from one coil do not link the other—and such is always the case—the total inductance, L_o, in the series-aiding case is less than four times the inductance of one coil and in the series-opposing case is greater than zero. But in any case the total inductance of two coils of any inductance connected in series-aiding will be given by $L_1 + L_2 + 2\,M = L_a$ and if they are connected series opposing the resultant inductance will be $L_1 + L_2 - 2\,M = L_o$. The following expression involving a new term, the **coefficient of coupling,** enables us to predict just what the total inductance in the circuit will be once we know how well the two coils are coupled.

The coefficient of coupling $\tau = M/\sqrt{L_1 L_2}$.

The coefficient of coupling depends upon the total inductance in the primary and secondary circuits as well as upon the mutual inductance between inductances A and B, Fig. 53.

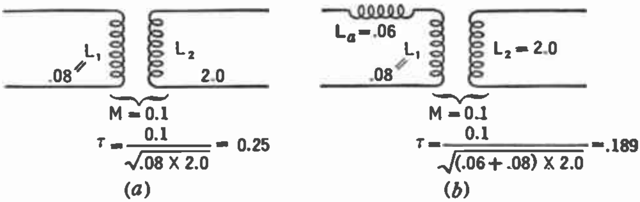


FIG. 53.—Examples showing dependence of coefficient of coupling on series inductance.

The mutual inductance depends upon only the two coils, A and B, and the coupling between them, or, $M = \tau\sqrt{L_1 L_2}$; the coefficient of coupling between two circuits depends upon the total inductance in the circuits. The maximum possible value of τ is 1.0. This is called unity coupling, and approaches this value in iron-core transformers. In air-core coils and transformers the coupling may be very "weak," that is, of the order of 0.1, and seldom gets as high as 0.7. In an iron core transformer 98 per cent coupling ($\tau = .98$) is usual.

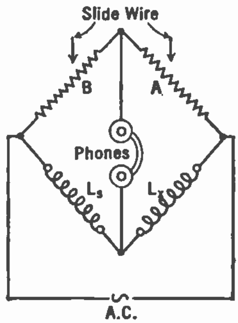


FIG. 54.—If A and B are so adjusted that there is no sound in the phones,

$$L_x = L_s \frac{A}{B}.$$

63. Measurement of inductance.—Inductance is usually measured by means of a Wheatstone bridge (Section 34) just as resistance is measured. This is essentially a method of comparing the unknown inductance to a known inductance. Resistances are used as the ratio arms, as in Fig. 54. When there is no sound in the telephones the inductances are equal if the ratio arms are equal, or if the ratio arms are not equal the unknown inductance is given by the equation, $L_x = L_s \frac{A}{B}$.

Mutual inductance is measured on a bridge, or by the following method: The inductance of the individual coils may be measured first. Then they are connected series aiding and the total inductance measured. This gives us the formula $L_1 + L_2 + 2M$, from which M can be calculated at once. Of course the same result will be obtained by connecting the coils series opposing. It is not even necessary to measure the individual inductances first, provided we can measure the inductance both series aiding (L_a) and then series opposing (L_o). Then

$$4M = L_a - L_o$$

$$M = \frac{L_a - L_o}{4}$$

Problem 3-4. In Fig. 55, when the coils are connected series aiding the inductance is measured to be 400 microhenries. What is the mutual inductance?

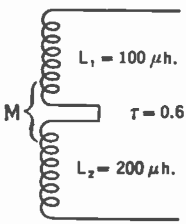


FIG. 55.—A problem in coupled circuits.

Problem 4-4. In Fig. 53 (*b*) calculate the coefficient of coupling if L_a is short-circuited, or removed from the circuit.

Problem 5-4. In a screen grid tube radio-frequency amplifier circuit the primary inductance is 350 microhenries, the secondary is 230 microhenries, the mutual inductance is 160 microhenries. Calculate the coefficient of coupling.

Problem 6-4. In Fig. 55, $L_1 = 100$ microhenries; $L_2 = 200$ microhenries, and $\tau = 0.6$. What is the mutual inductance? What is the total inductance ($L_o = L_1 + L_2 + 2M$)? What is it if L_2 is reversed (M is negative)?

64. The transformer.—A transformer is a device for raising or lowering the voltage of an a.-c. circuit. It "transforms" one voltage into another. It consists of two windings on an iron core, as in Fig. 56. The purpose of the iron core is to insure that the magnetic field set up about the primary will flow through the secondary coil without loss. What few lines of force do not link primary and secondary are called **leakage** lines and the inductance associated with them is called **leakage inductance.**

The primary is attached to an a.-c. line, the secondary to the load, whether this is a house lighting circuit, a motor, or any other device which requires electricity.

The lines of force from the continually changing primary alternating current flow through the secondary and induce voltages in it. A secondary current flows which *increases* when the primary current *decreases*, and which *decreases* when the primary current is *increasing*. If there are twice as many secondary turns as there are primary turns, the voltage developed across the secondary terminals will be double that across the primary. The following formula gives the relation between primary and secondary turns and the respective voltages:

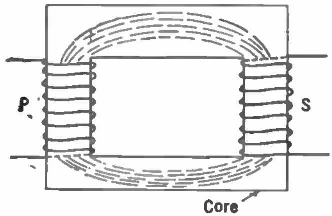


FIG. 56.—A simple transformer.

$$\frac{e_p}{e_s} = \frac{n_p}{n_s} = N \text{ (turns ratio).}$$

By using the proper ratio of turns, voltages either greater or less than the primary voltages may be secured at the secondary terminals.

Example 2-4. A transformer is to connect a 110-volt motor to a 22,000-volt transmission line. What is the ratio of turns between secondary and primary?

$$\frac{e_p}{e_s} = \frac{n_p}{n_s}$$

$$\frac{22{,}000}{110} = \frac{n_p}{n_s} = 200.$$

NOTE. This does not give the number of turns in either primary or secondary windings. The absolute number of turns depends on several factors; the ratio of turns depends on the voltages to be encountered.

Problem 7-4. In electric welding a very low voltage is used. What would be the turns ratio of a transformer to supply a welding plant with 5 volts if it takes power from the standard 110-volt circuit?

Problem 8–4. A transformer was used in the "old days" of radio when spark apparatus was standard equipment to step up the 110-volt circuit to approximately 30,000 volts. What was the turns ratio of the transformer?

Problem 9–4. A primary consists of 200 turns of wire and is connected to a 110-volt circuit. The secondary feeds a rectifier circuit requiring volts. How many turns will be on the secondary winding?

65. Power in transformer circuits.—Since the transformer not add any electricity to the circuit but merely changes or forms from one voltage to another the electricity that already exists, the total amount of energy in the circuit must remain same. If it were possible to construct a perfect transformer would be no loss in power when it is transformed from one vol to another. Since power is the product of volts times amperes, increase in voltage by means of a transformer must result in decrease in current, and vice versa. On the secondary side of transformer there cannot be more power than in the primary an if the transformer is one of high efficiency, the power will be slightly less than on the primary side. The product of am times volts remains the same.

Thus the primary power is

$$E_pI_p \qquad (1$$

and the secondary power is

$$E_sI_s \qquad (2$$

and since there is no loss or gain in power

$$E_pI_p = E_sI_s \qquad (3$$

when
$$\frac{I_p}{I_s} = \frac{E_s}{E_p} = N \text{ (turns ratio)},$$

which shows that the secondary voltage increases as N increases the secondary current decreases when N increases.

66. Transformer losses.—Transformers are not perfect. There is some resistance in both primary and secondary coils. The rent going through these resistances produces heat, which represents a certain amount of power lost. All of the lines of force coming out of the primary coil do not go through the secondary (the transformer does not have "unity coupling"). Some of the magnetic field of the primary, therefore, is not used in inducing currents in the secondary. The iron core—which is a metallic conductor in the magnetic field of the primary, just as the secondary wire is—has currents induced in it and since the iron is a high-resistance conductor it heats up. All of these losses must be supplied by the primary source of power, the generator. Large transformers, however, are very efficient, over 90 per cent of the input power being transferred to the secondary circuit.

67. The auto-transformer.—It is not necessary for proper transformation of voltage that the primary and secondary windings shall be distinct. In Fig. 57 is a representation of what is known as an auto-transformer, in which the secondary is part of the primary. The voltage across the secondary turns, however, bears the same relation to that across the primary part as though there were two separate windings. The ratio of voltages is the ratio of the number of turns possessed by the secondary and primary.

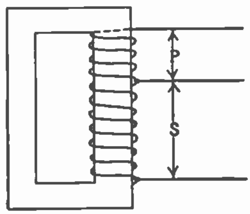


FIG. 57.—An auto-transformer. The secondary can be the entire winding or part as shown.

A transformer is often used when both alternating and direct currents flow through a circuit and it is desired to keep the direct current out of the circuit to which the secondary is attached. No d.-c. current can go across the transformer when the two windings are distinct, although the a.-c. voltage variations occurring in the primary are transferred to the secondary by the effects already described. If no increase or decrease in voltage is desired the turns ratio is made unity; that is, the same number of turns will be on the secondary as on the primary.

Such a case is an output transformer which couples a loud speaker to a power tube in a power amplifier. The power tube has considerable direct current flowing in its plate circuit in which the useful alternating currents also flow. The d.c. is undesirable in the loud-speaker windings, so a transformer is used to isolate the speaker from the d.c. of the tube. A good transformer of this type will transmit all frequencies in the audible range with an efficiency of about 80 per cent.

Problem 10-4. The line voltage in a certain locality is only 95 volts but a radio set is designed to operate from a 115-volt circuit. A transformer is to be used like that in Fig. 57. What will be the ratio of turns?

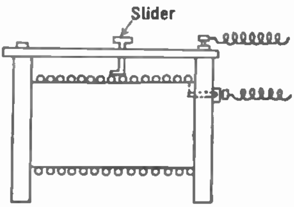


FIG. 58.—An early form of variable inductance for radio purposes called a "single slide tuning coil."

68. Transformer with open-circuited secondary.—When no current is taken from the secondary, the primary acts merely as a large inductance across the line. The current will be rather small. The energy associated with this current is used in two ways, one of which is in heating the transformer and its core. The other part maintains the magnetic field of the primary. This consumes

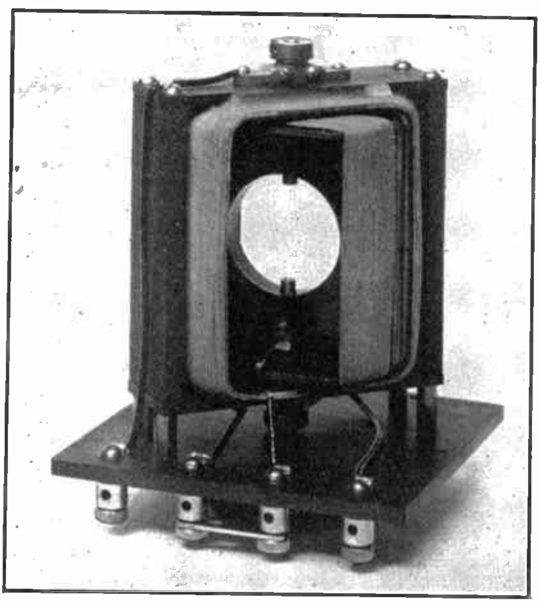


FIG. 59.—General Radio Company variable inductance.

no energy from the line because at each reversal of the current the energy of this field is given back to the circuit.

When the secondary load is put on, however, it begins to draw current from the secondary and more power is taken from the line leading to the generator. This additional power is that required by the load and the loss in primary and secondary resistance.

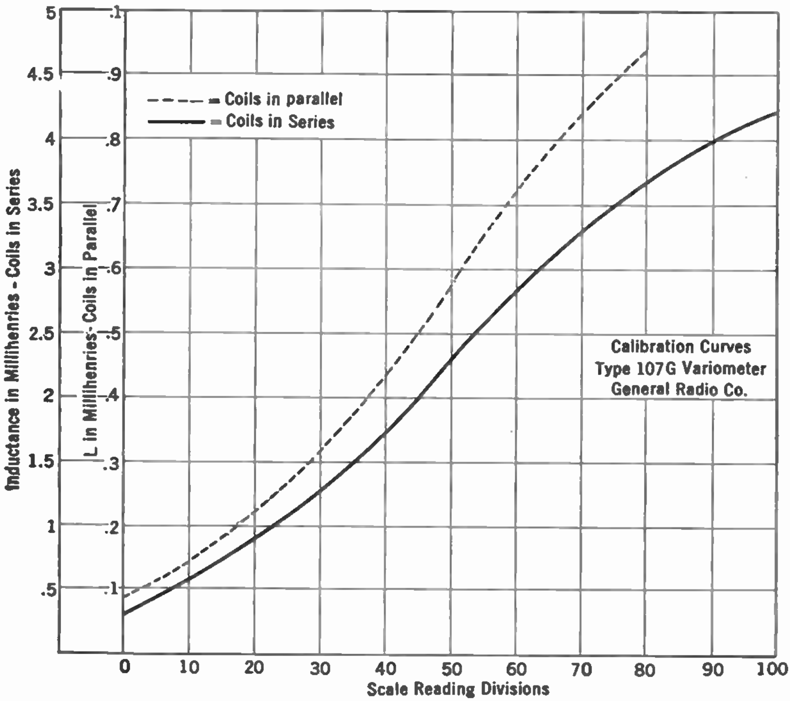


FIG. 60.—Calibration of a standard variable inductance.

69. Variable inductors.—A variable inductance may be used to regulate the current in an a.-c. circuit. This variation in inductance can be secured by means of a slider, as in Fig. 58, or by a fixed number of turns and a movable iron core. Variations in the position of the iron rod change the permeability of the core on which the wire is wound and thereby vary the inductance.

For radio-frequency work the variable inductance can take the form of a variometer, shown in Fig. 59, in which the inductance is continuously variable from a low value when the two coils are "bucking" each other, or are connected series opposing, to the maximum value where they are connected series aiding. The coils are always connected in the same manner, but by having one coil rotate within the other the variations in inductance result. The calibration of such a variometer is shown in Fig. 60.

70. Effect of current, frequency, etc., on inductance.—A good air core coil has constant inductance at all frequencies far from its natural frequency and at all currents through it. It can be measured at 1000 cycles on a bridge with the assurance that its inductance will not be different at radio frequencies.

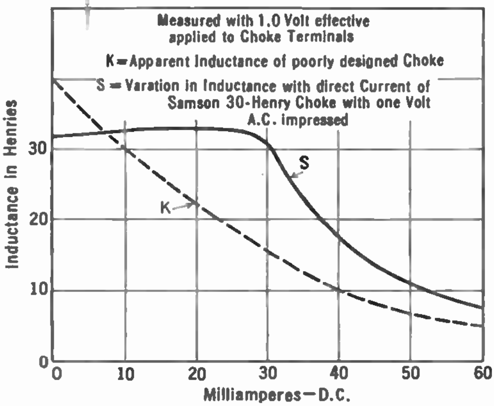


FIG. 61.—Inductance of iron core coils varies with d.-c. current because of variation in permeability.

When the current through an iron core coil changes, the inductance changes because of the change in permeability of the core. In order to keep the inductance more or less constant a small air gap is placed in the core. Curves indicating the inductance of a choke coil as the current through it is changed are shown in Fig. 61. The inductance of a coil to be used where both d.-c. and a.-c. currents are to flow through it should always be rated by considering the number of d.-c. amperes that are to flow through it. Thus a coil may be said to have 30 henries inductance at a d.-c. current of 30 milliamperes. This is the current at which it is supposed to be used. At other currents it may have more or less inductance.

The effect of leaving a small air gap in the iron core is shown in

Fig. 62. The air gap decreases the inductance at low values of d.-c. current but brings it up at high currents and thereby flattens the curve of inductance vs. d.-c. current.

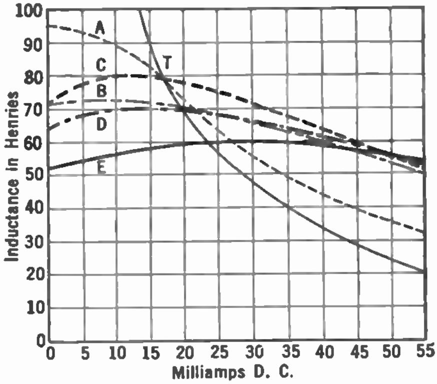


FIG. 62.—Variation of inductance with air gap.

T—no air gap.
A—average air gap.
B—air gap at one end, 0.01 inch.
C—air gap at both ends, 0.005 inch each.
D—air gap at both ends, 0.0075 inch each.
E—air gap at both ends, 0.01 inch each.

The effective inductance of coils changes greatly at some frequencies and in some circuits. At very high frequencies a coil may act more like a capacity because of the great number of turns between each of which exists some capacity. In high frequency transmitters or receivers, the choke coils to be used may arrive in the circuit by a cut-and-try method, calculations beforehand proving worthless.

CHAPTER V

CAPACITY

THERE are two essential electrical quantities in every radio circuit. These are **inductance** and **capacity.** They are represented in the circuit by the coils and the condensers. Upon their relative sizes depends the wavelength or frequency to which the receiver or transmitter is tuned. Resistance is always present too, but the effort of all radio engineers is to reduce the resistance and to overcome the losses in power due to its presence, just as mechanical engineers deplore the share of power wasted in mechanical friction.

71. Capacity.—Inductance has been likened to inertia. In an alternating-current circuit, it tends to prevent changes in the current flowing. Inductance is a property of a circuit; so is capacity. It is not something one can see, or feel, or hear; one cannot see, or feel, or hear electricity. We are only aware of it by the work it does. Inductance in concentrated form is possessed by coils. Whenever a coil has an alternating current flowing through it, the inductance is one of its important qualities. Capacity in concentrated form exists in condensers. Any two objects which are at different electrical pressure (e.m.f.) have a certain electrical capacity. This capacity tends to prevent any change in this electrical pressure or voltage which exists between these objects.

72. Capacity as a reservoir.—In an electrical circuit, a condenser serves the same purpose that the familiar standpipe or water tower serves in the water supply system of a city. The water tower maintains a constant water pressure regardless of the number of small drains from it, and regardless of the fact that the pumps filling the tower put water into it in spurts, not in a steady stream as comes from one's garden hose.

73. Capacity in a power supply device.—Alternating current taken from the house lighting wires may be put into a " rectifier " which cuts off half of the waves, as shown in Fig. 63. These spurts of current are forced through inductances which delay the rise of current to its final value on the half cycle in which current flows from the rectifier. On the other half cycle, in which no current flows from the rectifier the inductance tends to delay the decay of the current. The condensers which have been charged on the current half cycle discharge during the no-current half cycle. Current flowing into these condensers charges them to the voltage of the rectifier system. Then when the rectifier no longer passes current, the condensers begin to discharge and their voltage falls.

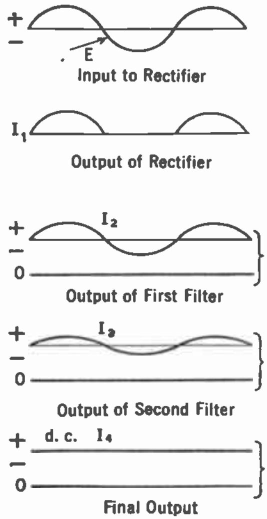


Fig. 63.—How the current in a "B eliminator" varies. The half waves from the rectifier are smoothed out by series inductances and parallel condensers until at I_4 it is pure direct current.

A proper combination of inductance and capacity, called a **filter**, will keep a perfectly steady current flowing out regardless of the fact that only spurts of current go into the system.

An inductance, then, opposes a change in current; it is like inertia in a mechanical system. Capacity opposes a change in voltage; it is like a reservoir. In an **inductive circuit** the current does not reach its maximum value until some time after the voltage has been applied. In a **capacitive circuit** the voltage does not rise to its maximum value until some time after the current has been flowing in it. A good condenser may keep charged with electricity for many hours after the charging voltage has been disconnected.

74. The charge in a condenser.—A condenser is made up of two or more conducting plates separated by a non-conductor. The

Leyden jar (Fig. 64) is a good illustration. Filter condensers used in B eliminators are made up of metal foil separated by waxed paper. The questions that everyone who looks at a condenser asks are these: Can a condenser pass an electric current? What is this capacity possessed by a condenser in concentrated form? How much capacity is in a condenser? What is the spark that jumps when a condenser is discharged?

When a condenser is connected to the terminals of a battery, a 45-volt B battery for example, there is a momentary rush of electrons on to one metallic condenser plate and an exit of electrons from the other. This constitutes a current flowing into the condenser, and if a voltmeter could be placed across it the voltage would be seen to rise in much the same manner in which the current builds up in an inductive circuit. As soon as the voltage of the condenser is the same as that of the battery, current no longer flows into it. It is now charged, and if the battery is disconnected the electrons remain on the one plate and there is a dearth of electrons on the other. Now if a wire is connected from one terminal to the other, these electrons jump across the gap in their effort to equalize the charge on the two plates.

Fig. 64.—A Leyden jar—an early form of condenser.

Once this spark has taken place the condenser is discharged.

So long as the condenser is charged it possesses energy, which is like the energy possessed by a ball on top a flag pole. The kind of energy possessed by the ball is potential energy; it is due to the position of the ball. The energy possessed by the condenser when charged is also **potential energy,** due to the strain existing in the non-conductor. Nothing happens until the condenser discharges, then it may set fire to a piece of paper, may puncture a hole in a sheet of glass, or may give some person a severe shock. Thus the condenser, just as the ball on top the pole, has the ability to do work—which is our definition of energy.

This is called **static** electricity, and is the same kind that produces sparks when we stroke the cat's back, or rub a comb on a coat sleeve, or the kind of electricity that jumps from one cloud to another on a hot summer day.

75. The quantity of electricity in a condenser.—The quantity of electricity that rushes into a condenser when it is connected to a battery is a perfectly definite quantity and can be calculated or measured. This quantity, Q, rated in **coulombs,** depends upon two factors only, the capacity of the condenser and the charging voltage. The **capacity** of the condenser depends only upon the physical make-up of the condenser, that is, (1) the size of the conducting plates, (2) the nature of the non-conductor called the **dielectric,** and (3) the distance apart of the plates. The quantity Q is proportional to both these factors, and may be expressed as

$$Q \text{ (coulombs)} = C \text{ (capacity)} \times E \text{ (voltage)}.$$

The unit of capacity is the **farad,** named from Michael Faraday, and is the capacity of the condenser whose voltage is raised 1 volt when 1 coulomb of electricity is added to it; or vice versa, the capacity of the condenser to which 1 coulomb of electricity can be added by an externally applied voltage of 1 volt. This is a very large unit and in practice engineers have to deal with millionths of farads, or microfarads. A smaller unit yet, micro-microfarad, is used in some radio circuits. This is equal to 10^{-12} farads. Another unit is the **centimeter of capacity.** It is equal to 1.1124 micro-microfarads.

We write the above expression as

$$C \text{ (farads)} = \frac{Q \text{ (coulombs)}}{E \text{ (volts)}}$$

This expression shows that the capacity of a condenser is the ratio between the quantity of electricity in it and the voltage across it.

The third way of stating the relation between capacity, quantity, and voltage, defines the voltage:

$$E \text{ (voltage)} = \frac{Q \text{ (quantity)}}{C \text{ (capacity)}}.$$

A discharged condenser, of course, has no electricity, Q, in it and hence no voltage across it. When it is connected to a battery, a voltage is built up across the two plates, the value of this voltage being given at any instant by the ratio between the quantity, Q, and the capacity, C, of the condenser. The greater the quantity of electricity stored on the conducting plates, the greater the voltage. When the battery is removed the quantity of electricity remains and, of course, a voltage, E, exists between the two plates.

76. Time of charge.—Since an ampere is a rate of flow of current, that is, 1 coulomb per second, one can calculate the rate at which current flows into a condenser provided the quantity, Q, and the time, t, are known. The amperes before the condenser is attached to the battery are zero, at the completion of the charging process the amperes are zero. The average rate, then, is what one secures from the equation,

$$I = \frac{Q}{t}.$$

Example 1-5. A condenser of 15 microfarads is attached to a 220-volt circuit. What quantity of electricity flows into it? If it requires 1/200 second to charge it, what is the average current?

$$\begin{aligned} Q &= C \times E \\ &= 15 \times 10^{-6} \times 220 \\ &= 3300 \times 10^{-6} \\ &= .0033 \text{ coulomb.} \\ I &= \frac{Q}{t} \\ &= \frac{.0033}{.005} \\ &= .66 \text{ ampere.} \end{aligned}$$

This is also the average rate of discharge if the time of complete discharge is 1/200 second.

Problem 1-5. What is the capacity of a condenser that holds .0024 coulombs when attached to 220 volts?

Problem 2-5. In a radio circuit is a .0005-mfd. (500 mmfd.) condenser across a 500-volt source. What quantity of electricity will flow into it?

Problem 3-5. What voltage will be necessary to put 0.012 coulomb into the condenser of Problem 1?

Problem 4–5. The average charging current in Problem 1 is 2 amperes. How long will it take to charge the condenser?

Problem 5–5. Suppose the average voltage across a condenser when it is being discharged is one-half the voltage when fully charged. Connect a 10-ohm resistance across the condenser of Problem 1. What average current flows? What is the average power used to heat the wire?

Problem 6–5. How long would it take to discharge the condenser in Problem 5? If the resistance is doubled, what power is used up in heat and how long will it take to discharge the condenser?

77. Energy in a condenser.—The amount of energy that can be stored in a condenser in the form of static electricity can be computed from the formula:

$$\text{energy} = \tfrac{1}{2} C E^2.$$

This represents the work done in charging the condenser, and naturally represents the energy released if the condenser is discharged.

Similarly, the energy in the lines of force about a coil through which an a.-c. current flows is equal to $\frac{1}{2} L I^2$.

The unit of energy or work is the **joule.** It is the amount of work required to force one coulomb of electricity through a one ohm resistance. Thus if a 1-mfd. condenser is charged to a voltage of 500, the energy is

$$\tfrac{1}{2} \times 1 \times 10^{-6} \times 500^2 = .125 \text{ joule.}$$

Since power is the rate of doing work, we can find the power required to charge such a condenser in one second of time by dividing the above expression by one second. Thus

$$\text{Power in watts} = \frac{1\,C\,E^2}{2\,t}$$

and if we attach the condenser to a secondary of a 500-volt transformer which charges the condenser 120 times a second (60-cycle current) the power will be $= \frac{1}{2} C E^2 \times 120$ provided the condenser is permitted to discharge each time. This proviso is true of the following discussion too.

A general expression for such a problem is

$$\text{Power} = \tfrac{1}{2}\, CE^2N,$$

if N is the times per second the condenser is charged and discharged.

Example 2–5. A condenser in a transmitting station has a capacity of .001 mfd. and is charged with a 20,000-volt source. What energy goes into the condenser and what power is required to charge it 120 times a second (60-cycle source)?

Energy or work, $W = \tfrac{1}{2}\, CE^2$

$= \tfrac{1}{2} \times .001 \times 10^{-6} \times 20{,}000^2$

$= 0.2$ joule.

Power, $P = W \times N$

$= \tfrac{1}{2}\, CE^2N$

$= 0.2 \times 120$

$= 24$ watts.

Problem 7–5. If the generator in the example above were a 500-cycle generator, what would be the power taken from it?

Problem 8–5. How much power is required to charge a 1-mfd. condenser to a voltage of 220, 120 times a second?

Problem 9–5. A transmitting antenna has a capacity of .0005 mfd. It is desired to transmit 1 kw. of power. To what voltage must the antenna be charged from a 500-cycle source?

Problem 10–5. Suppose an antenna is to be supplied with 500 watts of power and that between the charging mechanism and the antenna exists an efficiency of 30 per cent. The condenser, which discharges into the antenna, has a capacity of 0.012 mfd., and the generator which charges the condenser is a 500-cycle machine. A transformer is used to step up the voltage 110 from the generator to the value required by the condenser. What is the secondary voltage of the transformer and what is the turns ratio between secondary and primary? NOTE: Remember that a 500-cycle generator charges a condenser 1000 times a second. Answer; 15,200 volts, 131.

78. Electrostatic and electromagnetic fields.—The energy existing in an inductive circuit is said to exist in the electromagnetic field surrounding the inductance. This field is made up of lines of force and can be explored with a compass, or by sprinkling iron filings on paper as in Fig. 42.

The energy in a condenser is said to exist in the electrostatic field. This is the locality in which the electrical strain exists, that is, in the non-conductors in the vicinity of the conducting surfaces which are charged. This field cannot be explored with any magnetic substance, but can be discovered by any form of charged bodies or any container of static electricity.

Some circuits, an antenna system for example, have both capacity and inductance and, if properly charged, have both a magnetic and a static field. Since the wire can be charged to a very high voltage with respect to earth, considerably energy can be fed into it.

Frictional electricity, such as that produced by rubbing the cat's back, is a form of static electricity. It is this kind of electricity that is produced in the tank of a truck carrying gasoline along the road. The gasoline sloshing about in the metallic tank may raise the voltage of the tank to a considerable degree above the ground from which it is insulated by the rubber tires. Finally a spark may pass, and neutralize the charge—but in the process the tank and driver may be blown to bits. To prevent such accidents, all gasoline trucks trail an iron chain which connects the tank electrically with the ground and discharges it as fast as such static charges are produced.

79. Condensers in a.-c. circuits.—A perfect condenser is one which is an absolute non-conductor to d.-c. currents—that is, it is an infinite d.-c. resistance—and one which has no a.-c. resistance. All the power that is put into it is used in setting up an electrostatic field. Unfortunately all condensers have some a.-c. resistance, and few have infinite d.-c. resistance. Otherwise a condenser once charged would keep its charge forever. The time it takes a condenser to discharge is proportional to the product of its capacity and its resistance. This is known as its **time constant,** and is also the time required to charge the condenser. The resistance to d.c. is known as its **leakage resistance.** In a good condenser this may be as high as several hundred megohms.

Experiment 1–5. Charge a filter condenser of about 2- to 10-mfd. capacity by connecting to a 110-volt d.-c. circuit. Then discharge by a heavy wire; then charge again and allow to stand for a half-hour and discharge. Charge again and permit to stand for an hour and discharge. The relative sizes of spark give an idea of how poor a condenser it may be from the standpoint of leakage. Then charge and place a 10-megohm resistance across it for a second or so. Then see if it can be further discharged by means of a wire.

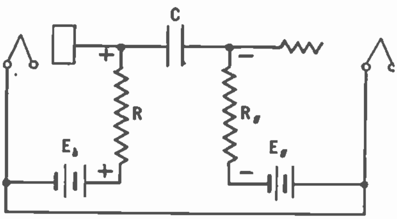


FIG. 65.—Leakage of current through the condenser C causes a voltage drop across the input of the following tube.

A good condenser may retain its charge for many hours after being removed from the source of charging current. The leakage of condensers not only takes place across the insulating material through which its terminals are brought out but through the wax filling, the container, and through the dielectric itself.

Example 3–5. In Fig. 65 is a typical coupling device used between tubes in a resistance-capacity coupled amplifier. A high-voltage battery is used. The purpose of condenser C is to keep these high d.-c. voltages from getting to the grid of the following tube. If this condenser has any leakage resistance, a d.-c. current flows through it and impresses a voltage on the grid of the succeeding tube which is highly detrimental.

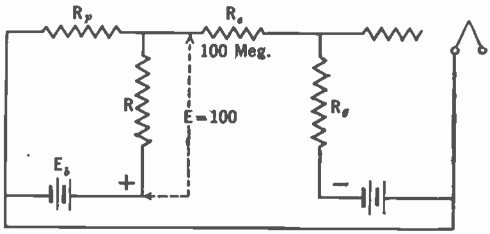


FIG. 66.—The circuit equivalent of Fig. 65.

Suppose the condenser has a resistance of 100 megohms. What voltage will be impressed on the grid if the battery has a voltage, E_b, of 200?

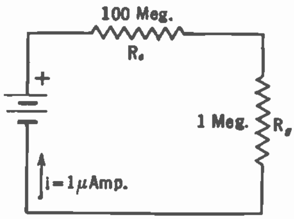


FIG. 67.—The battery in this figure represents the voltage across Rc and Rg in Fig. 65.

Figure 66 represents the circuit. It has the battery in series with two resistances, the plate resistance of the tube Rp and the coupling resistor R. Across Eb and R is shunted the condenser resistance and the grid leak in series. The problem is to find what current flows through this shunt circuit and what voltage drop this causes across the grid leak. Suppose 100 volts appear across the series circuit composed of Rc and Rg. This may be as represented in Fig. 67. One hundred volts across 100 megohms (the coupling resistance R and the grid leak resistance are negligible in comparison to the condenser leakage resistance) produces one microampere of current. This one microampere flowing through the grid leak of one megohm produces a voltage of 1 volt. This voltage is of a polarity that is opposite to the *C* bias and therefore decreases its value. In addition a certain amount of noise may be developed by the d.-c. current flowing through this condenser and grid leak. This noise is directly impressed on the input to the amplifier tube and may assume large values when amplified by succeeding stages. Condensers used in resistance amplifiers must have a high resistance.

80. Power loss in condensers.—A pure inductance takes no power from an a.-c. line once the magnetic field is established. If, however, the coil has resistance, power is wasted in heating it. Similarly, a perfect condenser, that is, one having no resistance, wastes no power. If the condenser has resistance—and all have—power is wasted in heat when it is connected to a source of current, whether a d.-c. or an a.-c. source. This power in watts is the current squared times the resistance.

81. Condenser tests.—If a voltmeter, a battery, and a condenser are connected in series a momentary deflection will be noted if the condenser is good. If the condenser is leaky, a constant deflection will be noted. If the condenser is fairly large, one or two microfarads, and no deflection is noted, the condenser is probably open. If the full battery voltage is read by the meter, the condenser is shorted.

If a condenser that has been determined to be not shorted is placed across a battery and then a pair of phones is placed across the condenser, a click will indicate that the condenser is good. The click is the discharge of the condenser through the phones.

82. Condensers in General.—A condenser, then, is any object with two or more conducting plates separated by a non-conductor called the dielectric. A cloud filled with moisture is a good conductor. So is the earth. The cloud may be a mile or so above the earth and subjected to all sorts of electrical differences of potential. It may become charged with respect to the earth. When this charge becomes great enough to jump the gap, a spark passes, and the condenser is discharged. This is known to us as lightning. Small discharges between parts of a cloud or between two clouds may cause only small sparks and are made known to us by "static."

The earth is considered as being at **zero potential.** All objects not connected to earth have a higher voltage than the earth, and hence any object has a capacity with respect to earth. This capacity will conduct electricity just as a one microfarad by-pass condenser in a radio receiver will, and may cause considerable embarrassment to the radio engineer or the experimenter who does not take it into consideration in his calculations.

In radio circuits the conducting plates of a condenser may be aluminum or brass or tin foil, depending upon the service which the condenser is to fill. The insulating plates, called the dielectric, may be air, oil, mica, coated paper coated with beeswax or other insulating compound. The actual capacity of the condenser may be fixed, or it may be variable.

83. The nature of the dielectric.—If two square metal plates 10 cm. on a side are suspended in air and about 1 mm. from each other, the capacity will be about 88.5 mmfd. If a sheet of mica is between the plates the capacity will be increased about eight times. Other substances will give different values of the capacity. Each substance, in fact, will give a certain value of capacity depending upon what is called the **dielectric constant** of the substance. The table below gives the value of K, the dielectric constant, of several substances.

This factor K has nothing to do with the ability of a substance to withstand high voltages without puncturing. Such ability differs not only with the substance but also with the condition of the substance at the time the voltage is applied, that is, the percentage moisture present, the pressure to which it is subjected, etc. Mica for example will withstand much greater voltages than paraffined paper.

Material	Dielectric Constant K	Material	Dielectric Constant K
Air	1	Paraffin	2
Bakelite	4 to 8	Porcelain	5 to 6
Celluloid	4 to 16	Rubber	2 to 3½
Glass	4 to 10	Pyrex	5.4
Mica	3 to 7	Shellac	3.5
Oil, castor	4.7	Varnished cambric	4
Oil, transformer	2.2	Wood	2 to 8
Paper	2 to 4		

84. Sizes of radio condensers.—The farad is a very large unit. In radio work the capacities used vary from a few million millionths of a farad to several millionths of farads. A millionth of a farad is known as a **microfarad,** and a millionth of this value is called a **micro-microfarad.** These are related as shown below.

One farad equals one million mfd. and one million million mmfd.
One mfd. equals one millionth farad and one million mmfd.
One mmfd. equals one million millionth farad, and one millionth mfd.

Sometimes the centimeter is used as a unit of capacity. It is equal to 1.1124 micro-microfarads.

85. Condenser capacity formulas.—Formulas have been worked out by which it is possible to compute the capacity of condensers of various forms. For example the capacity of two flat conducting plates separated by a non-conductor may be computed from the formula:

$$C = \frac{885 \times A \times K}{10^{10} \times d},$$

where C = capacity in microfarads;
A = area of the metallic plate in square centimeters;
K = dielectric constant of the non-conductor;
d = thickness of dielectric in centimeters.

Or

$$C = 0.0885 \frac{KA}{d}$$

where C = capacity in micro-microfarads;
d = thickness in centimeters;
A = area in square centimeters;
K = dielectric constant.

Formulas for other types of condensers may be found in the Bureau of Standards Bulletin 74, Radio Instruments and Measurements, page 235.

In receiving sets the tuning condensers are variable. The important function of separating one station from another is performed by changing the capacity of the condenser, which is called tuning the circuit. The tuning condensers have air as the dielectric and plates of various metals, usually brass or aluminum. The capacities range from 25 mmfd. to 100 mmfd. in a short-wave (high-frequency) receiver to 500 mmfd. for broadcast frequency receivers. Receivers for the long waves used in transoceanic communications are much larger. The above values of capacity may be written as .0001 and .0005 mfd. It is probably easier to express small capacities in micro-microfarads rather than in one of the larger units. Whenever an easy path for an alternating current is needed a fixed condenser is used. It is called a **by-pass** condenser.

Example 4–5. How many plates 16 × 20 cm. in area and separated by paraffined paper ($K = 2\ 1$) .005 cm. thick are required for a condenser of 24 mfd.?

$$C = \frac{885\,AK}{10^{10}\,d}$$

$$= \frac{885 \times 16 \times 20 \times 2.1}{10^{10} \times .005}$$

$$= 0.0119 \text{ mfd. capacity per plate.}$$

$$\text{Number of plates} \quad = \frac{24}{.0119} = 2200.$$

Problem 11–5. Express in micro-microfarads: $\frac{1}{1000}$ farad, 1 mfd., 0.00025 mfd. Express in farads: 500 mmfd., 0.01 mfd., $\frac{1}{10}$ mfd. Express in microfarads: 1 farad, 500 mmfd., 0.01 mmfd.

Problem 12–5. What is the capacity of two square plates suspended in air 0.1 mm. apart, if the plates are 10 cm. on a side?

Problem 13–5. A variable tuning condenser has a capacity of 0.001 when air is used as dielectric. Suppose the container is filled with castor oil. What is the capacity now?

Problem 14–5. Lead foil plates are separated by mica 0.1 mm. thick having a dielectric constant of 6. What is the capacity of a condenser made up of 200 pairs of such plates?

Problem 15–5. How many joules of energy can be stored in such a condenser as in Problem 14 when 100 volts are impressed across it? How much power will it take to charge it to this voltage 120 times a second?

86. Condensers in series and parallel.—When condensers are connected in parallel (Fig. 68) the resultant capacity is the sum of

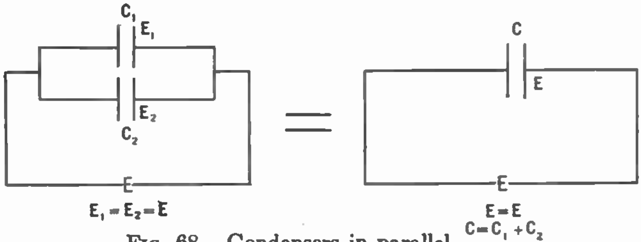


Fig. 68.—Condensers in parallel.

the individual capacities. When they are in series (Fig. 69) the resultant may be found as below:

$$C_{\text{parallel}} = C_1 + C_2 + C_3 \ldots .$$

$$C_{\text{series}} = \cfrac{1}{\cfrac{1}{C_1} + \cfrac{1}{C_2} + \cfrac{1}{C_3} \ldots .}$$

The resultant of two capacities in series is

$$C_{\text{series}} = \frac{C_1 \times C_2}{C_1 + C_2}.$$

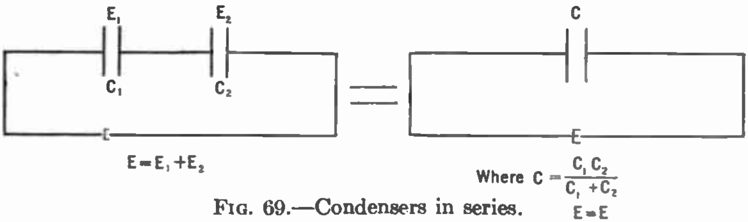


Fig. 69.—Condensers in series.

In the parallel case the same voltage is across each capacity. In the series case the voltage varies inversely as the capacity. If two equal capacities are in series half the total a.c. voltage is impressed across each condenser. If one condenser has half the capacity of the other, that one will have two-thirds the total voltage whereas the other will have one-third the total voltage across it.

The resultant capacity of several condensers in parallel is always greater than any single capacity; in series the resultant is less than the capacity of the smallest of the group. In series the voltage across each condenser varies inversely as its capacity and is always less than the total voltage across the combination. When a condenser is placed in an a.-c. circuit whose voltage is more than the condenser can tolerate, it is only necessary to use two or more condensers in series so that the voltage across individual members of the group is below the danger limit, and so that the total capacity in the circuit is the value desired.

When condensers are used across d.-c. circuits, as in filter circuits, the d.-c. resistance of the condenser becomes of importance. If two condensers in series across a certain d.-c. voltage have equal capacities but different d.-c. resistances, the voltage drop across the two condensers will differ. The voltage across one of them may be sufficient to destroy it.

Example 5–5. In a radio circuit a .0005-mfd. variable condenser is available but the circuit calls for a .00035-mfd. condenser. What fixed condenser may be used to reduce the maximum capacity in the circuit to the proper value? How shall it be connected?

Solution. Since the total capacity is to be reduced, the fixed condenser must be connected in series with the variable condenser. The total capacity is given as 0.00035 mfd. This is equal, from the above equation, to

$$.00035 = \frac{C_1 \times C_2}{C_1 + C_2}$$

$$= \frac{.0005 \times C_2}{.0005 + C_2}$$

whence $C_2 = .001166$ or 1166 mmfd.

Problem 16–5. In a transmitter a " blocking " condenser is needed whose capacity must be approximately 0.001 mfd. The voltage it must stand is 1000. A 0.002 condenser is available which can stand only 400 volts. What size condenser must be used in series so that no more than 400 volts is across the 0.002 condenser? (Neglect resistance of condensers.)

Problem 17–5. Whenever the capacity of a tuning circuit is quadrupled, the inductance remaining constant, the wavelength is doubled and the frequency is halved. A broadcast receiver tunes to 600 meters (500 kc.) with a 500-mmfd. condenser. What maximum capacity must be put in parallel with this condenser in order to receive 800-meter (375-kc.) radio compass signals and ship-to-shore traffic on 2,200 meters? Ans. 390 mmfd., 6250 mmfd.

CHAPTER VI

PROPERTIES OF ALTERNATING-CURRENT CIRCUITS

The two kinds of current in common use are: **direct currents** (d.c.) which have a more or less constant value and which flow in the same direction all the time; and **alternating currents** (a.c.) in which not only is the magnitude constantly changing but the direction also.

87. Definitions used in a.-c. circuits.—When the voltage (or current) has started from zero, risen to its maximum value in one direction, decreased to zero and risen to maximum value in the opposite direction and finally come back to its starting value and point, zero, it is said to have completed a **cycle**. Ordinary house-lighting current which has a frequency of 60 cycles per second goes through this cyclic change in magnitude and direction 60 times a second. The **frequency** is the number of times a second a cycle is completed. An **alternation** is half a cycle; that is, when the voltage has gone from zero to zero through one maximum it is said to have completed one alternation. In 60-cycle circuits there are 120 alternations per second. In a.-c. circuits we must consider the element of time; in d.-c. circuits time does not enter; the magnitude of the current is constant.

Alternating currents exist of nearly all ranges of frequencies. Sixty cycles is the common power frequency; tones generated by audio-frequency oscillators for testing purposes may go from almost zero frequency to as high as the human ear can hear, that is, about 13,000 cycles per second depending upon the person. Electric waves of frequences as low as 15,000 cycles exist. They are generated in the long wave high-power radio stations carrying on transoceanic communication. From that value radio frequencies exist up to about 30,000,000 cycles per second. This corresponds to a wavelength range of from 20,000 meters to 10 meters.

88. Instantaneous value of alternating current.—Since the voltage (or current) is continually changing in value it becomes expedient to provide a means of knowing what this value is at any time.

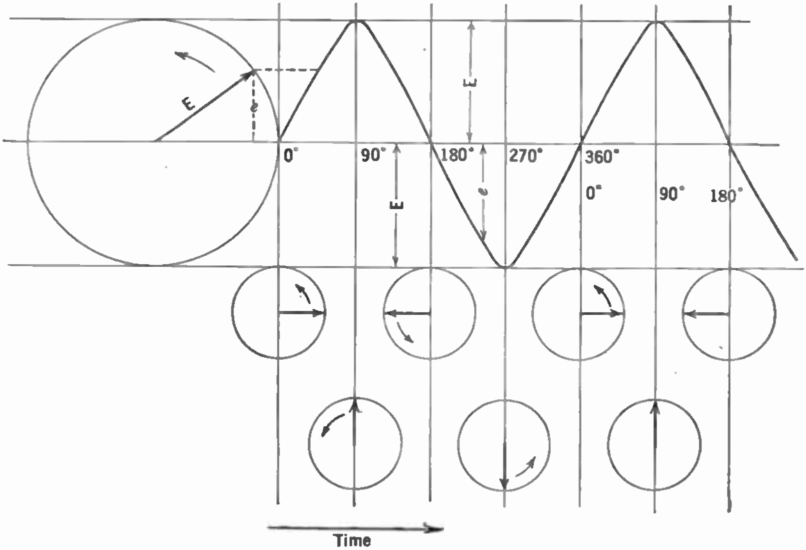


FIG. 70.—As the vector *E* rotates, the circle moves to the right. A piece of crayon attached to the end of the vector would trace out a curve similar to the wavy line. When the vector has the position as shown in the first small circle, the instantaneous value *e* is zero. At other times the instantaneous voltage has some other value.

Let us consider the circle of Fig. 70 which is moved to the right at a constant rate. Within the circle is a rotating arm, representing the motion of the rotating part of an a.-c. generator, as well as the voltage, *E*, it produces. It rotates at a constant speed such that one full rotation—one cycle—is completed in the time it takes the circle to move to the right a distance equal to the diameter. Now, when the arm is perpendicular to its starting position, the circle has completed one-quarter of its movement; when the arm is pointing in a direction opposite to its starting position the circle has moved through one-half of its motion, and so on. Now let us picture what the end point of the arm would trace out if we attached a crayon to it and let it go through its motion as the circle is moved to the right. Such a tracing will be an accurate representation of an alternating current or voltage.

In Fig. 70 the height of the arm above the horizontal axis, its starting position, represents the value of the voltage at the instant the generator winding is at the position in its cycle corresponding to the position of the rotating arm whose length is E. The position of the arm at any point is known as its **phase.** Since a cycle is represented by a complete circle of 360 degrees (360°), when the arm is vertical we speak of its position at the 90° phase. Now the height of this arm from the horizontal starting position is the value of the a.-c. voltage at that position or phase or instant of time. At 90 degrees this height is equal to the length of the arm itself, or the a.-c. voltage is at its maximum value; at any other point in that half-cycle or alternation the voltage is less than this value.

Now it is handy to have something to which to compare the value of the voltage at any phase, known as the **instantaneous** value—because this value is only temporary due to rotation of the alternator armature. This basis of reference is the **maximum** or **peak** value. The instantaneous value is always rated by stating its magnitude with respect to the maximum value. Fortunately there is a factor which relates the height of the arm representing the instantaneous value and its length, or maximum value. This factor is known as the **sine** of the angle between the arm and the vertical line. Knowing the maximum value of an a.-c. voltage—the length of the rotating arm in Fig. 70—and the phase, or the angle through which the arm has rotated, to determine the instantaneous value of the voltage we need only multiply the maximum value by the sine of this angle which we may look up in a table made out for such a purpose. For example, the functions of several angles are given below. The angle itself (which is a means of expressing the time that has elapsed since the alternator arm started rotating) is called the **phase angle.**

Angle Degrees	Sin	Cos	Tan
15	.259	.966	.268
30	.500	.866	.577
45	.707	.707	1.000
60	.866	.500	1.732
90	1.000	.000	∞
110	.940	− .342	−2.747
135	.707	− .707	1.000
175	.087	− .996	0.087
180	.000	−1.000	.000
220	− .643	− .766	+ .839
270	−1.000	− 000	∞
300	− .866	+ .500	−1.732
360	.000	+1.000	.000

88a. Triangle functions.—Considering the angle between CB and AB in Fig. 71 labeled as θ (the Greek letter theta), the side AC is called the **opposite** side, CB is called the **adjacent** side. Then these relations hold:

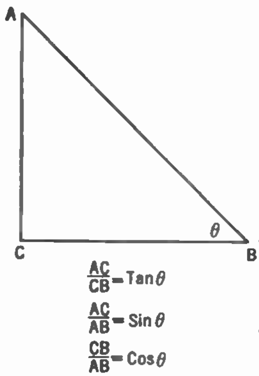


FIG. 71.—Trigonometric "functions."

$$\frac{AC}{CB} = \tan\theta \qquad (1) \qquad \text{or } AC = CB\tan\theta$$

$$\frac{AC}{AB} = \sin\theta \qquad (2) \qquad \text{or } AC = AB\sin\theta$$

$$\frac{CB}{AB} = \cos\theta \qquad (3) \qquad \text{or } CB = AB\cos\theta$$

Knowing any two of the three functions of the right-angled triangle and the angle involved, the other function may be found by means of the table in Section 88.

NOTE. The terms "sine," "cosine," etc., are called the functions of the angles.

The function of angles greater than 90° may be found from. function $(N \times 90° + A)$ = function A, if N is even, e.g., sin 210° = sin $(2 \times 90° + 30°)$ = sin 30°. Function $(N \times 90° + A)$ = cofunction A if N is odd, e.g., sin 120° = sin $(1 \times 90° + 30°)$ = cos 30°.

89. Means of expressing instantaneous values.—We may express the instantaneous value of an a.-c. voltage or current as follows:

$$e = E \sin \theta \quad \text{or} \quad i = I \sin \theta,$$

where e or i = the instantaneous value;
E or I = the maximum value;
θ = the phase angle in degrees.

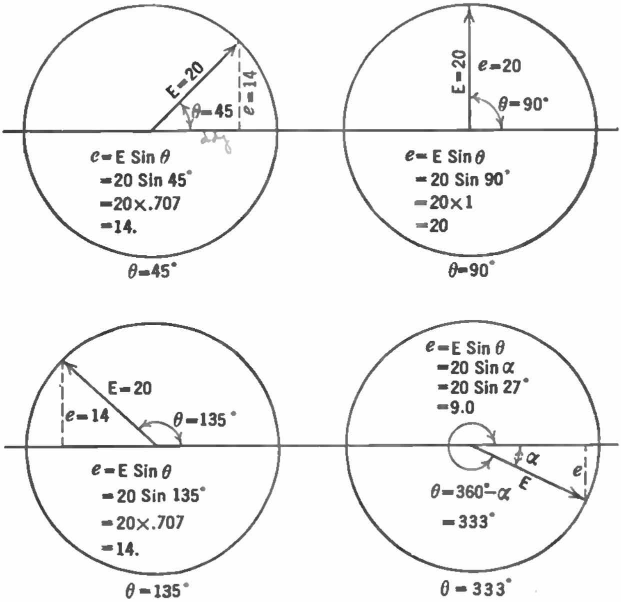


FIG. 72.—At various times in the cycle the instantaneous value of the vector E is as shown in these vector diagrams.

Small letters denote instantaneous values, capital letters denote maximum values.

Let us look at Fig. 72 which represents the rotating arm E and the vertical height e in four typical cases, 45°, 90°, 135°, and 333°. The actual height compared to the maximum length of the arm E may be calculated by means of the above table and formulas.

Since the sine of an angle of 0 degrees is zero, the instantaneous value of the voltage at 0 phase is zero; since the sine of an angle of 90° is 1, the instantaneous value of the voltage at this point in the cycle is equal to the maximum value; and so on.

The three methods of representing an a.-c. voltage or current are:

1. By a graphical illustration such as Fig. 70, called a sine wave.

2. By an equation, such as

$$e = E \sin \theta \quad \text{or} \quad i = I \sin \theta.$$

3. By the pictures shown in Fig. 72, known as **vector diagrams.** Such a line as E in Fig. 73 which moves about a circle is called a **vector**; the vertical distances of its end point from the horizontal axis is called its **vertical component.** The angle θ between the horizontal and the vector is called the **phase angle**; the value of the vertical component may be found by multiplying the maximum value E by the sine of the phase angle.

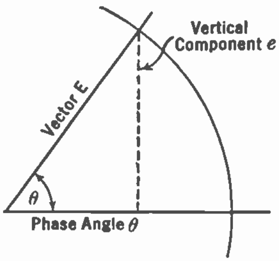


FIG. 73. — The maximum value of the vector is E; the instantaneous value is e.

Example 1–6. Represent a voltage whose maximum value is 20 volts. Using graph or cross-section paper twelve divisions to the right equals one alternation and ten divisions vertically up and down from our horizontal line represents the maximum values of the voltage. The voltage starts at zero, increases to a maximum at 90° or six divisions, then decreases to zero at twelve divisions, etc. What is its value at other times? We can tell by using our table of sines in Section 88. At the 30° phase the instantaneous value, or the height of rotating arm above the time axis, is $e = E \sin 30° = 20 \times .5 = 10$ volts. Other instantaneous values can be found similarly and the entire sine wave plotted similar to Fig. 70.

Lay off on cross-section paper a length say 20 divisions equal to the maximum value of the voltage. Then using this value as a radius draw a circle.

Then the instantaneous value at any time in the cycle can be found by measuring the vertical distance of this point on the circle to the horizontal axis. Thus at the 30° phase the vertical distance is 10 because sin 30° = .5 This illustrated the vector diagram.

A voltage of maximum value 20 may be represented mathematically as

$$e = 20 \sin \theta$$

Problem 1–6. The maximum value of an alternating voltage is 110. What is its value at the following phases: 30°? 60°? 110°? 180°? 270°? 300°? 360°?

Problem 2–6. The instantaneous value of an alternating voltage is 250 volts at 35°. What is its maximum value? What is its value at 135°?

Problem 3–6. The instantaneous value of an alternating voltage is 400 volts at 75°. Plot to some convenient scale its sine wave.

Note. In all this discussion voltages or currents can be spoken of with the same laws in mind. Thus the form of a sine wave of current looks exactly like the sine wave of voltage with the same maximum value. The vector diagram looks the same because it is only necessary to label the rotating arm I instead of E and the mathematical formula reads $i = I \sin \theta$ instead of $e = E \sin \theta$. The answers to the above problems will be the same numerically whether we speak of voltage or current.

A word should be said, too, about the terminology frequently used in speaking of the voltages and currents in an a.-c. circuit. Engineers use the expression "a.-c. voltage" or "a.-c. current" for simplicity, not stopping to think that such an expression really is an abbreviation for "an alternating-current voltage" or for "alternating-current current." Although one would not say the latter, one often uses the abbreviation. In many radio circuits there are both a.-c. and d.-c. branches and in some or all of them both direct and alternating currents and voltages exist. It is simpler to speak of an "a.-c. voltage" than of an alternating e.m.f. and in the interest of simplicity this terminology has been employed here whenever it is useful.

90. Effective value of alternating voltage or current.—Since the voltage (or current) in an a.-c. system is rapidly changing direction, and since the needle and mechanism of an ordinary d.-c. measuring instrument require appreciable time for a deflection, they cannot follow the rapid changes of voltage or current and would only wobble about the zero point of the meter even if they could follow the fluctuations. We can, however, compare direct and alternating currents by noting their respective heating effects. An alternating current is said to be equal in value to a direct current of so-many amperes when it produces the same heating effect. This is known as the **effective value** of the alternating current and is equal to the maximum values multiplied by .707 or divided by $\sqrt{2}$.

Thus $$I_{\text{eff.}} = .707\, I = I/\sqrt{2} \quad \text{or} \quad I_{\text{eff.}} = \frac{I}{1.41}$$

where $I_{\text{eff.}}$ = effective value of an alternating current;
I = maximum value.

The effective value is also known as the **root mean square** or r.m.s. value for the following reasons. The heating effect of a direct current is proportional to the square of the current. Then if we take the instantaneous values of the current over a cycle of alternating current, square them, get an average of these values, extract the square root of this value, it will be equal to the direct-current value that will produce an identical heating effect. The value of current secured in this manner is .707 times the maximum value. Since it is the "square root of the average or mean squares" of several current values, it is abbreviated to the "root mean square" or r.m.s. An r.m.s. voltage is one that will produce a current whose heating effect is the same as a given direct current as discussed above.

$$E_{\text{r.m.s.}} = E_{\text{eff.}} = .707\, E_{\text{max.}} = \frac{E_{\text{max.}}}{\sqrt{2}}$$

and

$$E_{\text{max.}} = \frac{E_{\text{eff.}}}{.707} = E_{\text{eff.}} \times \sqrt{2}.$$

Voltage or current is considered as effective unless otherwise indicated or stated.

Example 2–6. What is the effective value of an alternating voltage whose maximum value is 100 volts?

$$E_{\text{eff.}} = .707 \times 100 = 70.7 \text{ volts}$$

Problem 4–6. The effective value of an alternating current is 12 amperes. What is the maximum value?

Problem 5–6. The maximum value of an alternating voltage is 110 volts. What it the effective value? 110 × .707 = 77 volts.

Problem 6–6. At the 45° phase the instantaneous value of an a.-c. alternating current is 10 amperes. What is its effective value?

Problem 7–6. The effective value of an alternating current is 100 milliamperes. What is the instantaneous value at the 60° phase?

91. Phase relations between current and voltage.—Whenever an a.-c. voltage forces a current through a resistance, the wave form of the voltage and the current, the mathematical formula for them, and the vector diagrams look alike. This is explained by the fact that the current and voltage start at the same instant, rise to a maximum value at the same instant and carry on throughout their respective cycles in perfect step, or **in phase.**

When an inductance or a capacity or any combination of these quantities with each other or with resistance is in the circuit, other phenomena take place differing entirely from what happens in a d.-c. circuit. For example, when an a.-c. voltage forces a current through an inductance, the current does not attain its maximum value at the same instant as the voltage, but at a later time; when the inductance is replaced by a capacity, the opposite is true, the maximum value of the current takes place before the maximum voltage is reached.

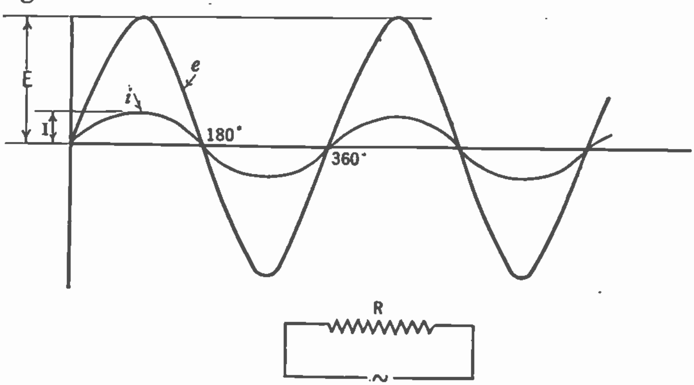


Fig. 74.—Current and voltage in phase.

92. Case I. *Current and voltage in phase.*—Figure 74 represents the current and voltage in phase, i.e., in a resistive circuit. Since the form of the voltage and current waves is exactly similar they can be drawn on the same horizontal axis, or in the vector diagram can be represented as in Fig. 75. They can be thought of as two vectors, which may or may not have the same length, rotating at the same speed in two different circles which move forward in the same direction at the same speed. Under these conditions, the end point of the vectors will trace out identical curves.

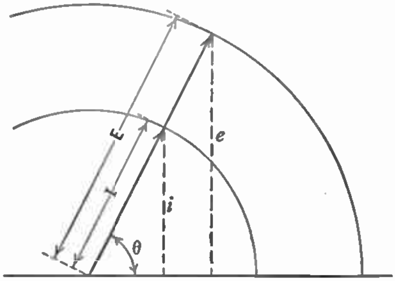


FIG. 75.—Current and voltage in phase. The maximum value of voltage greater (or drawn to different scale) than the maximum value of the current.

In such cases Ohm's law $I = E/R$ tells us the relations between current, voltage, and resistance, just as it does in a d.-c. circuit.

Example 3–6. Suppose a lamp of 55 ohms is placed across a 110-volt 60-cycle a.-c. line. What current will flow through it at the 30° phase?

We must first find the maximum value of the voltage.

$$E = E_{\text{eff.}} \times \sqrt{2}$$
$$= 110 \times 1.41 = 155 \text{ volts.}$$

Since there is no phase effect in the circuit due to the resistance, the current is given by Ohm's law

$$I = E/R$$
$$= \frac{155}{55} = 2.82 \text{ amperes.}$$

This is the maximum current. The current at any phase may be found by

$$i = I \sin \theta$$
$$= 2.82 \sin 30°$$
$$= 2.82 \times .5 = 1.41 \text{ amperes.}$$

Problem 8–6. A resistance of 10 ohms is in a circuit with an alternating voltage of 20 volts maximum. At what phases will the current through the resistance be 1 ampere?

Problem 9–6. A certain alternating current has the same heating effect as a direct current of 8 amperes. It flows through a resistance of 25 ohms. What is the effective and maximum voltage? At what phases will the instantaneous value of the voltage be equal to one-half the maximum value?

93. Case II. *Current lagging behind the voltage.*—Let us consider the case where the current does not attain its maximum value at the same instant that the maximum voltage is reached, as is illustrated in Fig. 76. It will be noted that the current curve does not start until 67.5° of the voltage curve has been completed, and therefore that the maximum value of the current is said to lag behind the voltage maximum 67.5°. The current and voltage in

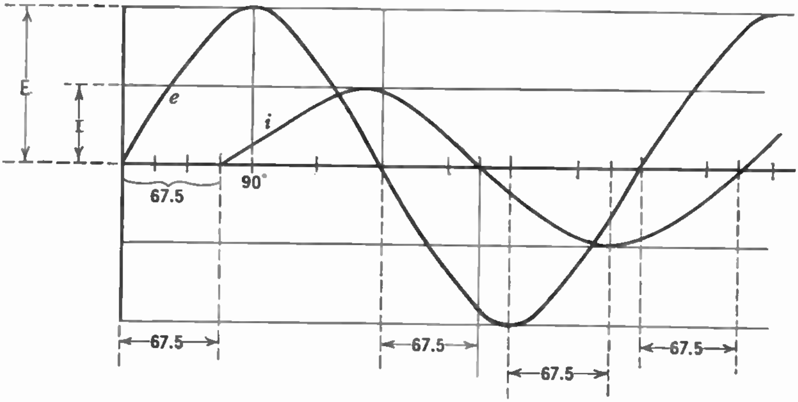


Fig. 76.—Current and voltage in an inductive circuit where the current lags behind the voltage.

such a case may be thought of as two vectors, or arms, moving in two circles one of which, the current circle, does not start until the other or voltage circle has completed 67.5° of its total movement of 360°.

The formulas for Case II where the current is lagging are

$$e = E \sin \theta,$$

$$i = I \sin (\theta - \phi),$$

where θ = phase of the voltage in degrees;

ϕ = difference in phase between E and I or the angle of lag. (The angle ϕ is called "Phi.")

Example 4–6. The current lags behind the voltage by 60°. The maximum value of the current is 40 amperes. What is the instantaneous value of the current at the 75° phase?

Solution. Lay off on graph paper the voltage at the 75° phase and 60° behind it the current which has a maximum value of 40 amperes. The vertical component then is equal to the instantaneous value of the current at this phase.

The problem may also be solved by the mathematical formula

$$\begin{aligned} i &= I \sin (75° - 60°) \\ &= 40 \sin (75° - 60°) \\ &= 40 \sin 15° = 40 \times .26 = 10.4. \end{aligned}$$

Problem 10–6. If the maximum voltage is 110 what is the instantaneous voltage at the 110° phase? At the 90° phase? At 45°?

Problem 11–6. In an inductive circuit there is a phase difference of 25°. When the voltage is a maximum, the instantaneous value of the current is 10 amperes. What is the maximum value of the current?

The cause of lagging current is inductance, which tends to make the maximum of current take place later than the maximum of voltage. If a circuit is purely inductive (the resistance is negligible) the difference between these maxima is 90°. If there is appreciable resistance the difference is less than 90°.

94. Inductive reactance.—The opposition to the flow of current which inductance imposes on a circuit is called the **inductive reactance** and is measured in ohms just as resistance is. Its abbreviation is X_L. In any circuit in which there is only resistance, the expression which connects voltage and current is the familiar Ohm's law,

$$\text{current} = \frac{\text{voltage}}{\text{resistance}} \quad \text{or} \quad I = \frac{E}{R}.$$

Similarly, the expression when inductance is in an a.-c. circuit is

$$\text{current} = \frac{\text{voltage}}{\text{reactance}} \quad \text{or} \quad I = \frac{E}{X_L},$$

and if the voltage is the maximum value the current will be the maximum value; if the voltage is the effective or r.m.s. value, the current will be the effective value; if the voltage is the instantaneous value the current will be the instantaneous value.

Inductive reactance is numerically equal to

$$X_L \text{ (ohms)} = 6.28 \times f \times L = \omega L$$

where f = frequency in cycles per second;
L = inductance in henries;
ω = Greek letter omega = $6.28 \times f$.

Example 5–6. In an a.-c. circuit the following data are given: $E_f = 110$ volts; inductive reactance, $X_L = 20$ ohms. Find the maximum and effective current and the instantaneous current at the 150° phase?

Solution. The effective current is found from

$$I_f = \frac{E_f}{X_L}$$

$$= \frac{110}{20} = 5.5 \text{ amperes.}$$

$$I_{\max} = I_f \times 1.41 = 7.8 \text{ amperes.}$$

The vector diagram in Fig. 77 shows the instantaneous current to be

$$\begin{aligned} i &= I \sin (\theta - 90°) \\ &= 7.8 \sin (150° - 90°) \\ &= 7.8 \sin 60° \\ &= 7.8 \times 0.866 \\ &= 6.75 \text{ amperes.} \end{aligned}$$

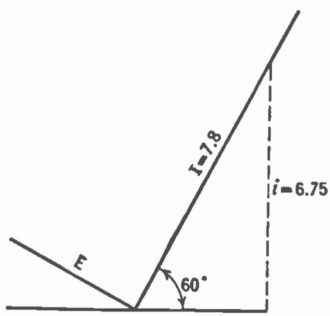


FIG. 77.—Current lagging behind the voltage by 90°.

Problem 12–6. In the above example find the instantaneous voltage when the instantaneous current is 6 amperes. At what phase is this?

Problem 13–6. What inductive reactance is needed to keep the maximum current down to 75 amperes in a 110-volt circuit?

Capacit.

95. CASE III. *Current leads the voltage.*—In this case the maximum value of the current is reached before the corresponding maximum voltage is reached. The voltage lags behind the current, or as it is usually stated, the current **leads** the voltage. A vector diagram for such a case is shown in Fig. 78.

In this case the instantaneous values of voltage and current are:

$$e = E \sin 60^\circ$$

$$i = I \sin 80^\circ \quad \text{or} \quad i = I \sin (60^\circ + 20^\circ)$$

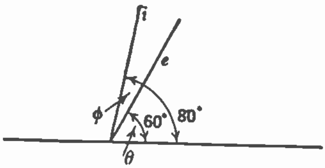


FIG. 78.—Current leading the voltage by the angle ϕ at the 60° phase. The angle of lead is 20°.

The formulas for Case III when the current leads the voltage are

$$e = E \sin \theta,$$

$$i = I \sin (\theta + \phi),$$

where ϕ is phase difference between E and I or the angle of lead.

The current in such an equation will be the maximum current if the voltage is maximum, effective if the voltage is effective, etc.

Example 6–6. The effective current in an a.-c. circuit is 70 amperes. The angle of lead is 30°. What is the instantaneous current when the voltage is at the 10° phase?

The maximum value of the current is found from

$$\begin{aligned} I_{max} &= I_{eff} \times 1.41 \\ &= 70 \times 1.41 \\ &= 98.7 \text{ amperes.} \end{aligned}$$

By the equation

$$\begin{aligned} i &= I \sin (\theta + \phi) \\ &= 98.7 \sin (10^\circ + 30^\circ) \\ &= 98.7 \times .643 \\ &= 64.5 \text{ amperes.} \end{aligned}$$

Problem 14–6. The instantaneous value of current in a certain capacitive circuit is 8 amperes. The instantaneous value of the voltage is 25. The maximum values of the current and voltage are 15 amperes and 80 volts respectively. What is the angle of lead between them?

96. Capacity reactance.—The opposition which a condenser offers to the flow of current in an a.-c. circuit is called its **capacitive**

reactance and is measured in ohms just as resistance and inductive reactance are. The equation

$$\text{current} = \frac{\text{voltage}}{\text{capacitive reactance}} \quad \text{or} \quad I = \frac{E}{X_c}$$

is similar in form to Ohm's law and the equation for current in an inductive circuit.

Capacitive reactance is equal numerically to

$$X_c(\text{ohms}) = \frac{1}{6.28 \times f \times C} = \frac{1}{\omega C}$$

where f = frequency in cycles per second;
C = capacity in farads;
ω = Greek letter omega = $6.28 \times f$.

Current leads the voltage in a capacitive circuit because capacity tends to prevent any changes in voltage and so the maximum of current in a purely capacity circuit takes place 90° ahead of the maximum of voltage. If there is a appreciable resistance in the circuit the difference is less than 90°; thus resistance tends to bring the current and voltage in phase.

Example 7–6.—If a condenser which has a capacity reactance of 5 ohms, is in an a.-c. circuit the instantaneous value of the voltage at the 20° phase is 48 volts. What is the maximum current through the condenser? What is the instantaneous current through it at the 20° phase?

Solution.

$$e = E \sin 20°$$
$$48 = E \times .342$$
$$E = 140 \text{ volts}$$
$$I = \frac{E}{X_c}$$
$$= \frac{140}{5} = 28 \text{ amperes}$$
$$i = I \sin (20° + 90°)$$
$$i = 28 \sin 110°$$
$$= 28 \cos 20°$$
$$= 28 \times .940$$
$$= 26.32 \text{ amperes.}$$

Problem 15-6.—If a condenser in an a.-c. circuit whose voltage is 110 passes a current of 3 amperes what is the reactance of the condenser in ohms?

Problem 16-6.—Condensers are usually rated at the maximum voltage at which they can be operated with safety. What should be the rating of a condenser to be used in a 220-volt a.-c. circuit?

Problem 17-6.—An a.-c. circuit has a voltage of 115, and a current of 4.5 amperes is flowing. It has a condenser in it. What is the reactance of this condenser? What is the instantaneous value of the current when the voltage is 80 volts? At what phase is this?

97. Comparison of inductive and capacitive reactances.—Coils and condensers have opposite effects upon an alternating current. The reactance of an inductance increases with increase of frequency; a condenser has less reactance as the frequency increases.

A coil which will pass considerable current at 60 cycles may pass practically none at one million cycles. Where it is desired to pass a low-frequency current and to prevent the passage of a high-frequency current, an inductance in series with the circuit may be used. Note that the coil—called a **choke coil**—is in series with the circuit, where a by-pass condenser would be across the circuit. If even greater discrimination against a high-frequency current is desired, a combination of condenser and choke is used. The choke is in series, the condenser is shunted across the circuit.

Example 8-6.—Assume an a.-c. circuit composed of an inductance of one millihenry. What current will flow if E is 100 volts and the frequency is 600 cycles?

$$X_L = 6.28 \times f \times L$$
$$= 6.28 \times 1 \times 10^{-3} \times 600$$
$$= 3.8 \text{ ohms}$$

$$I = \frac{E}{X_L} = \frac{100}{3.8} = 26.3 \text{ amperes.}$$

When it is desired to exclude current of a given frequency from a circui a shunt capacity is placed across the circuit. High frequencies will go this **by-pass** condenser whereas the lower frequencies will not be so shun and will go on through the rest of the circuit. A frequent use is where R.F. choke passes direct current but prevents the flow of alternating current whereas a condenser passes a.c. but stops d.c. A large condenser is pl across batteries so that a.-c. currents will have an easy path around

Example.—What is the reactance of a 500-mmfd. condenser to radio waves of a frequency of 600 kilocycles?

$$X_c = \frac{1}{6.28 \times 600 \times 10^3 \times 500 \times 10^{-12}}$$

$$= \frac{10^9}{6.28 \times 600 \times 500}$$

$$= \frac{10^5}{6.28 \times 30} = \frac{10^5}{188.4} = 530 \text{ ohms.}$$

Problem 18–6.—What would the current be if the frequency were 6000 cycles? 60 cycles? If the inductance were one henry? One microhenry? Assume $E = 100$.

Problem 19–6.—Calculate the reactance of one henry, one millihenry, one microhenry at the following frequencies: 100 cycles, 1000 cycles, 1,000,000 cycles.

Problem 20–6.—What reactance is needed to keep the current into an electric iron down to 5 amperes when it is placed across a 110-volt circuit (assuming the iron has no resistance)?

Problem 21–6.—The inductance in an a.-c. circuit is .4 henry. At what frequency will the current be 3 amperes if the voltage is 110?

Problem 22–6.—Calculate the reactance of a 1-mfd. 0.001-mfd., 50-mmfd.-condenser at 60 cycles, 60,000 cycles, 600 kc., 15,000 kc.

Problem 23–6.—The capacity in an a.-c. circuit is 1.0 mfd. At what frequency will the current through it be 415 milliamperes if the voltage is 110?

98. Measurements of capacities.—Condensers may be measured for capacity by comparing them with a known capacity by means of a Wheatstone bridge. In this case the unknown capacity may be calculated from

$$C = \frac{B}{A} C_s,$$

which differs from the formula when resistances or inductance are measured because of the fact that the reactance of a condenser decreases the larger it is. The formula when inductances are compared is:

$$L = \frac{A}{B} L_s.$$

The capacity of condensers from 0.01 to 10 or more microfarads may be measured by noting the current through them with a known voltage across them. The condenser is first tested for open or short as indicated in Section 81. Then, in series with a milliammeter, the condenser is plugged into a light socket (a.-c. of course). Then the voltmeter may be put across the condenser, in case the voltage of the line is not known. The capacity is

$$C \text{ mfd.} = \frac{I \text{ ma.} \times 1000}{6.28 \times f \times E}.$$

99. Combinations of resistance with capacity or inductance.—Coils and condensers are never pure reactances. They always have some resistance in them, although in most radio apparatus the resistance is negligible compared to the reactance. Since a reactance as well as a resistance impedes the flow of current, we must combine them to determine what current will flow through a piece of apparatus under a certain voltage and at a certain frequency.

Because an inductance has a different effect upon an a.-c. current than a resistance, and different from capacity, we cannot merely add their reactances in ohms to determine the resultant effect upon the circuit. They must be added *vectorially*, not *algebraically*.

100. Impedance.—Combinations of resistance and reactance are called **impedances.** The value in ohms may be found as follows: Two factors whose effect is at right angles to each other may be combined and the resultant secured by the formula found in plane geometry which states that "the square on the hypotenuse of a right triangle is eoual to the sum of the squares on the other two sides." Thus

$$Z^2 = R^2 + X^2,$$

and if $R = 3$ ohms and $X = 4$ ohms,

$$Z^2 = 9 + 16 = 25,$$

whence

$$Z = \sqrt{25} = 5.$$

This is called getting the **vectorial** sum. The **algebraic** sum, obtained by simple addition—as when two resistances are combined—would be, in this case, 7 ohms whereas the vectorial sum is 5 ohms.

The resultant of combining a resistance and a reactance can be found graphically. Lay off on a horizontal line a number of units corresponding to the number of ohms resistance. Then if the reactance is inductive, erect a perpendicular and lay off on it a number of units equal to the number of inductive reactance ohms. The length of line connecting the extremities of these two lines is the resultant impedance in ohms.

Because capacitive reactance has an opposite effect to that of inductive reactance, the line representing it should be pointed downward. Graph paper is of great aid in solving a.-c. problems in this manner.

Example 9–6.—An alternating current of 8 amperes maximum flows through a coil whose inductance is 0.043 henry and whose resistance is 5 ohms. What voltage is required if the frequency is 60 cycles?

The current in such a circuit is

$$I = E/Z$$

$$Z = \sqrt{R^2 + X^2}$$

and

$$X = 2\pi f \times L = 6.28 \times 60 \times .043 = 16.25 \text{ ohms}$$

$$Z = \sqrt{5^2 + 16.25^2} = \sqrt{289} = 17 \text{ ohms}$$

whence

$$E = IZ = 17 \times 8 = 136 \text{ volts.}$$

Example 10–6.—What is the impedance in a circuit in which there is a condenser of 1.66 mfd. and a resistance of 800 ohms? The frequency is 60 cycles.

$$Z = \sqrt{R^2 + X_c^2}$$

$$X_c = \frac{1}{2\pi fC}$$

$$= \frac{10^6}{6.28 \times 1.66 \times 60} = 1590 \text{ ohms}$$

$$Z = \sqrt{800^2 + 1590^2}$$

$$= \sqrt{(64 \times 10^4) + (256 \times 10^4)} \quad \text{(approx.)}$$

$$= 10^2\sqrt{320}$$

$$= 1790 \text{ ohms.}$$

101. General expressions for impedance.—If an a.-c. circuit is composed of resistance and both inductive and capacitive reactance the impedance is figured as follows. Since the inductive and capacity reactances are opposite in effect, the negative sign is fixed to the capacity reactance, the positive sign to the inductive reactance. That is, a capacity reactance is a negative reactance of so-many ohms; an inductive reactance is a positive reactance as so-many ohms. Before they are combined with the resistance vectorially, their algebraic sum is obtained. Thus the general expression for impedance is

$$Z = \sqrt{R^2 + (X_L - X_C)^2},$$

and after the capacity reactance has been combined with the inductive reactance (it is actually subtracted because the signs of the two reactances are different) the form of the impedance becomes as before,

$$Z = \sqrt{R^2 + X^2}.$$

It will be noted that the sign before X^2 in the above equation is positive. This is always the case since two negative quantities multiplied together (or if a negative quantity is squared) result in a positive quantity. If, for example, the actual value of the capacity reactance in ohms was greater than the inductive reactance in ohms, the effective reactance in the circuit would be negative but X^2 would be positive.

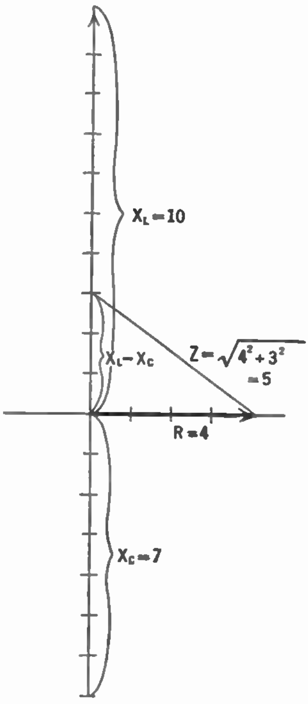


FIG. 79.—Vector diagram of a circuit containing resistance (4 ohms) capacity reactance (7 ohms) and inductive reactance (10 ohms).

Example 11-6.—What is the impedance of a circuit consisting of a capacity reactance of 7 ohms, an inductive reactance of 10 ohms and a resistance of 4 ohms?

The vector diagram of such a case is shown in Fig. 79. Here we have X_L pointing upward at an angle of 90° from the resistance and X_c pointing downward at an angle of 90° from the resistance. The total effect of the reactances is 10 − 7 or a positive 3 ohms which points upward.

If, however, the values of X_L and X_c are interchanged, so that the resultant of adding the reactances is a negative 3 ohms which point downward, then

In Case I,
$$Z = \sqrt{R^2 + (X_L - X_c)^2}$$
$$= \sqrt{4^2 + (10 - 7)^2}$$
$$= \sqrt{4^2 + 3^2} = 5.$$

In Case 2,
$$Z = \sqrt{R^2 + (X_L - X_c)^2}$$
$$= \sqrt{4^2 + (7 - 10)^2}$$
$$= \sqrt{4^2 + (-3)^2}$$
$$= \sqrt{4^2 + 3^2}$$
$$= 5.$$

Problem 24-6.—An antenna (Fig. 80) may be considered as an inductance, L_a and a condenser in series. If the voltage in Fig. 80 is 100 microvolts f = 1000 kc., what is the current through the coil L_s in series with L_a? (There is no mutual inductance between L_a and L_s.)

Problem 25-6.—What is the effective reactance in a circuit which has 45 ohms inductive reactance, 70 ohms capacitive reactance and 20 ohms resistance? What is the impedance? What current would flow if the voltage were 110 effective?

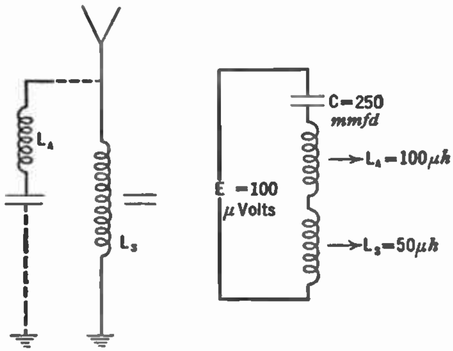


FIG. 80.—An antenna and its equivalent.

Problem 26-6.—What would be the values of capacity and inductance if the frequency were 500 cycles?

Problem 27-6.—What voltage is required to force one milliampere through the following circuit: Resistance 8 ohms, inductance 300 microhenrys, capacity 500 mmfd., frequency 750 kc.?

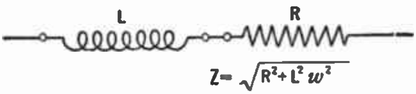


FIG. 81.—A series circuit: $\omega = 6.28 \times f$.

102.—Series a.-c. circuits.—In Fig. 81 is an inductance in series with a resistance. The current flowing in the circuit may be found by dividing the voltage across the circuit by the impedance of the circuit. That is: $I = E/Z$, in which

$$Z = \sqrt{R^2 + X^2},$$

which is quite different in numerical value from $R + X$. For example, if $R = 3$ and $X = 4$, the vector sum $Z = 5$ where as the arithmetical sum $= 7$.

As in a d.-c. circuit, the voltage across an impedance, a reactance, or a resistance is equal to that impedance, reactance or resistance in ohms times the current in amperes.

Voltage across a resistance	$E_R = I \times R$
Voltage across an inductance	$E_L = I \times X_L$
Voltage across a capacity	$E_C = I \times X_C$
Voltage across L and C	$E_{L+C} = I\,(X_L - X_C)$

The voltage across two resistances or reactances is the *algebraic* sum of the individual voltages, remembering that a capacity reactance has a negative sign and that the voltage across it is negative with respect to that across an inductance. The voltage across two impedances, however, must be determined by adding the individual voltages *vectorially*. This is because the impedance is a vector sum of a resistance and reactance.

Let us take a typical example. The current in the circuit of Fig. 81 is

$$I = \frac{E}{\sqrt{R^2 + X^2}}$$

or

$$E = I\sqrt{R^2 + X^2}$$

$$E^2 = I^2\,(R^2 + X^2)$$

or

$$E^2 = I^2R^2 + I^2X^2$$

$$= E_R^2 + E_X^2$$

whence

$$E = \sqrt{E_R^2 + E_X^2}$$

Therefore the resultant voltage across a resistance and a reactance is the vector sum of the individual voltages.

Example 12–6.—If $E = 15$, $R = 3$, $X = 4$

$$I = \frac{15}{\sqrt{R^2 + X^2}} = \frac{15}{\sqrt{9 + 16}} = \frac{15}{5} = 3 \text{ amperes}$$

$$E_R = IR = 3 \times 3 = 9 \text{ volts}$$
$$E_X = IX = 3 \times 4 = 12 \text{ volts}$$
$$E = \sqrt{E_R^2 + E_X^2} = \sqrt{81 + 144} = \sqrt{225} = 15$$

Experiment 1–6.—To measure the capacity of a condenser. Place a condenser of about 10-mfd. capacity in series with an a.-c. milliammeter and measure the current through it when placed across a 110-volt, 60-cycle line.

Then $$E = IX_c = I \times \frac{1}{6.28 \times f \times C}$$

or $$C = \frac{I}{E \times 6.28 \times f}$$

where E = line voltage

or $$C \text{ mfd.} = \frac{I}{41.5} = I \times .024$$

when $E = 110$;
$f = 60$;
I = milliamperes.

103. Phase in series circuit.—In a resistive circuit, the voltage and current are in phase, their maximum values occurring at the same instant. If the circuit is purely capacitive, or inductive, there is a 90° phase difference between current and voltage.

If, instead of a pure reactive circuit, we have some resistance, the angle of lead or lag (Sections 93, 95) is not 90° but is some value less than this. To determine the phase angle, or the difference in phase, let us draw the vector diagram of the voltages as in Fig. 82. The voltage across the resistance, IR, is the horizontal line, and at an angle of 90° with it is the voltage across the reactance, IX. The diagonal of the parallelogram represents the resultant voltage across the impedance, IZ.

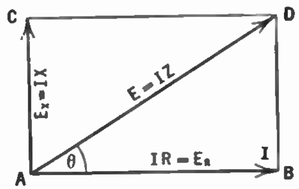


Fig. 82.—The length of the line AD represents the vector voltage across an inductance and a resistance in series.

Because a resistance in an a.-c. circuit produces no phase difference between the current and voltage the current through and the voltage across a resistance are said to be in phase. Their directions may be represented along the same line, that is, along the horizontal line representing the voltage across the resistance IR. The direction of the diagonal represents the direction of the voltage across the entire circuit. Since, then, the direction of the IR line represents the direction of the current, I, and the direction of the IZ line represents the direction of the voltage, E, the angle between these lines represents the angular difference in phase between the voltage and current. The angle θ then is equal to the angle of phase difference between the voltage across the combination and the current through it. Thus, in Fig. 82 $BD \div AB$ is the tangent of the angle θ, or

$$\frac{BD}{AB} = \tan \theta,$$

and since $BD = AC = IX$ (or the voltage across X) and $AB = IR$ (or the voltage across R),

$$\frac{E_X}{E_R} = \frac{IX}{IR} = \frac{X}{R} = \tan \theta.$$

Knowing the reactance and the resistance in ohms the tangent of the angle may be determined, and the angle itself looked up in a table. When the tangent of an angle is known but not the angle, the expression is written $\theta = \tan^{-1} \frac{X}{R}$ and is read "θ (theta) the the angle whose tangent is X over R."

The effect of a resistance in series with a reactance is to decrease the angle of phase difference between the current and the voltage or to bring them more nearly in phase. In a pure reactance circuit, the angle is 90°; when resistance is added this angle decreases. In a pure resistance circuit, there is no angle, the current and voltage are in phase; they reach their maximum values at the same instant.

Example 13–6.—In an a.-c. circuit there is a resistance of 10 ohms and an inductive reactance of 8 ohms. A current of 8 amperes is flowing. What voltage exists across each part of the circuit and across the entire circuit? What is the phase difference between the current and the voltage?

$$\text{Voltage across } R = IR = 8 \times 10 = 80 \text{ volts}$$
$$\text{Voltage across } X = IX = 8 \times 8 = 64 \text{ volts}$$

Draw the vector diagram to scale as in Fig. 83; then the diagonal IZ = 102.5 volts. (Note that the algebraic sum of the voltages across R and X is 144 volts.) The tangent of the angle of phase difference is equal to $X \div R$ or

$$\tan \theta = X/R = 8/10 \text{ or } .8$$
$$\theta = \tan^{-1} .8$$

or

$$\theta = 38° \, 40'$$

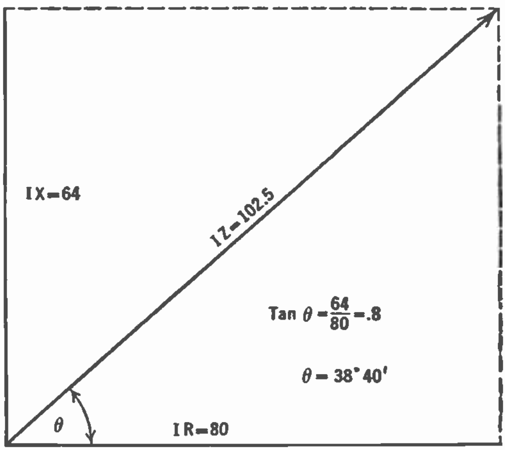


FIG. 83.—A vector diagram of problem 13.

104. Characteristics of a series circuit.—1. The voltage across a series combination of resistance and reactance is the vector sum of the voltages across the separate units.

2. The combined resistance of several resistances in series is the algebraic sum of the individual resistances.

3. The combined reactance of several reactances, whether inductive or capacitive, is the algebraic sum of the individual reactances.

4. The impedance, or combined effect of a resistance and reactance, is the vector sum of their individual values.

5. The combined impedance of several separate impedances is the vector sum of the individual impedances.

Example.—Suppose we combine two resistances, reactances, etc., of 3 and 4 ohms respectively. The table below shows the resultant values.

Combination	Sum		Resultant
1. $R = 3$; $X = 4$	$\sqrt{9 + 16}$	$= Z$	5
2. $R = 3$; $R = 4$	$3 + 4$	$= R$	7
3. $X_L = 4$; $X_c = 3$	$4 - 3$	$= X$	1
3. $X_L = 3$; $X_c = 4$	$3 - 4$	$= X$	−1
3. $X_L = 3$; $X_L = 4$	$4 + 3$	$= X$	7
3. $X_c = 3$; $X_c = 4$	$-4 - 3$	$= X$	−7
4. $R = 3$; $X = 4$	$\sqrt{9 + 16}$	$= Z$	5
(1) $R = 3$, $X_L = 4$ $X_c = 3$	$\sqrt{9 + (4 - 3)^2}$	$= Z$	3.16
(2) $R = 3$, $X_L = 3$ $X_c = 4$	$\sqrt{9 + (3 - 4)^2}$	$= Z$	3.16
(3) $R = 3$, $X_L = 3$ $X_c = 3$	$\sqrt{9 + (3 - 3)^2}$	$= Z$	3

Note in (1) and (2) above that the resultant is the same although the conditions are different. This is due to the fact that a negative number when squared, or multiplied by itself, becomes a positive number. In other words, a negative reactance and a resistance always produce a positive impedance.

105. Resonance.—In (3) above, a very important phenomenon is illustrated. When the capacity reactance of a series circuit equals the inductive reactance, their respective effects cancel out and the resultant impedance is the resistance in ohms alone. To a circuit possessing inductive reactance one can add a certain amount of capacity and thereby reduce the impedance of the circuit (at some particular frequency) to the value of the ohmic resistance. This is the phenomenon underlying all tuning in radio circuits; it is known as **resonance.** √

Problem 28–6.—Two resistances, one of 8 ohms and the other of 24 ohms, are in a 60-cycle 110-volt circuit. What current flows? What is the current if the frequency is increased to 500 cycles?

Problem 29-6.—What current exists in the above-named circuit if the second resistance is replaced by an inductive reactance of 24 ohms? If the frequency is 60 cycles what inductance will be in the circuit?

Problem 30-6.—In a circuit with 550 volts across the terminals are the following pieces of apparatus: A coil with 15 ohms reactance, a condenser with 7 ohms reactance, two resistances of 10 and 5 ohms. What current flows? What is the voltage across each part? What is the phase relation between voltage and current?

Problem 31-6.—In an a.-c. circuit appear a voltage across a resistance of 34 volts and a voltage across a capacity of 66 volts. What is the voltage across the combination?

Problem 32-6.—Two condensers are in series with two inductances and a resistance. The condensers have reactances of 8 and 10 ohms, the inductances 20 and 6 ohms, and the resistance is 4 ohms. What current flows, what voltage appears across each component and what is the phase between current and voltage? Assume $E = 110$.

Problem 33-6.—What is the phase difference in the following cases: (a) pure resistance circuit; (b) pure inductive circuit; (c) pure capacity circuit; (d) 100 ohms resistance and 100 ohms inductive reactance; (e) 100 ohms resistance and 50 ohms inductive reactance; (f) 100 ohms resistance and 100 ohms capacity reactance; (g) 100 ohms resistance and 50 ohms capacity reactance; (h) 100 ohms inductive reactance and 50 ohms resistance and 25 ohms capacity reactance; (i) 100 ohms each inductive and capacitive reactance and 100 ohms resistance?

Problem 34-6.—In a series circuit there are 45 ohms inductive reactance and 20 ohms resistance. It is desired to increase the phase angle between the current and voltage to 85°. How can this be done? How can the phase angle be decreased to 30°?

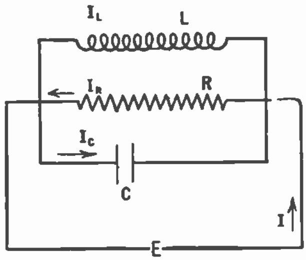


FIG. 84.—In a parallel circuit the current I may be very small compared to I_L or I_C.

106. Parallel circuits.—In a circuit like that of Fig. 84, in which several reactances or combinations of reactance and resistance may be connected in parallel, the following rules hold:

The *voltage* across each branch equals the voltage across the combination.

The *current* through the combination is the vector sum of the currents through each branch.

The *impedance* offered to the flow of current by the combination is the voltage divided by the total current.

Thus in Fig. 84 the current through the entire combination may be found as follows, assuming $E = 120$; $X_C = 8$; $X_L = 5$; $R = 3$:

$$I_C = \frac{E}{X_C} = \frac{120}{8} = 15 \text{ amperes through the condenser}$$

$$I_R = \frac{E}{R} = \frac{120}{3} = 40 \text{ amperes through the resistance}$$

$$I_L = \frac{E}{X_L} = \frac{120}{5} = 24 \text{ amperes through the inductance}$$

$$I = \sqrt{I_R^2 + (I_L - I_C)^2} = \sqrt{1681} = 41 \text{ amperes}$$

$$Z = \frac{120}{41} = 2.92 \text{ ohms.}$$

107. Phase in parallel circuit.—The phase angle between the current and the voltage in a parallel circuit may be obtained from the expression

$$\tan \theta = \frac{I_L - I_C}{I_R}$$

or

$$\theta = \tan^{-1} \left(\frac{I_L - I_C}{I_R} \right)$$

108. Impedance of parallel circuit.—Since the impedance is the ratio between the voltage across the circuit and the current through it, in order to find the impedance of several branches in parallel we must know the voltage and the current. Often we would like to know the impedance without knowing either the voltage or the current. The procedure then is to assume a voltage, to find the currents that would flow, divide the voltage by the current and get therefrom the impedance, or

$$Z = \frac{E}{I}.$$

Example 14-6.—What is the impedance of 630 ohms capacity reactance shunted by 100 ohms of resistance?

Assume a voltage of 100.

$$I_C = 100/630 = .159 \text{ ampere}$$
$$I_R = 100/100 = 1.0 \text{ ampere}$$
$$\text{Total current } I = \sqrt{I_C^2 + I_R^2}$$
$$= \sqrt{.159^2 + 1^2} = \sqrt{1.025}$$
$$= 1.015 \text{ amperes}$$
$$Z = \frac{E}{I} = \frac{100}{1.015} = 98.5 \text{ ohms.}$$

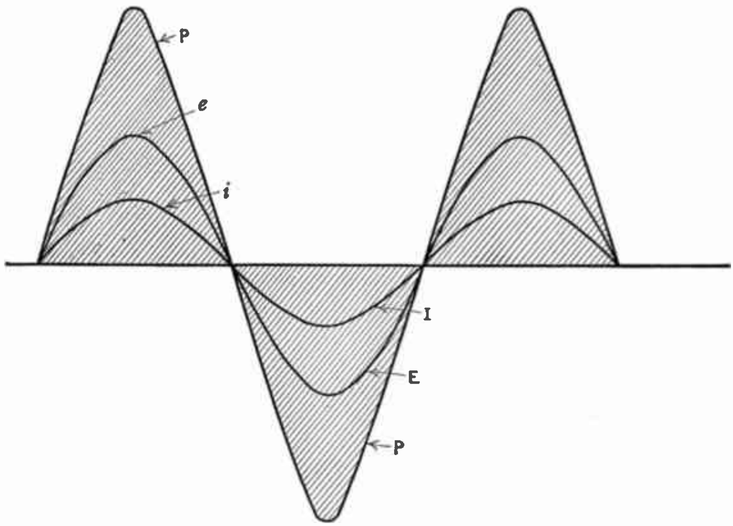


FIG. 85.—All the power in a resistive circuit is used up.

109. Power in a.-c. circuits.—In a d.-c. circuit the power is the product of the voltage across the circuit and the current through it. Thus, if one ampere is fed into a device under a pressure of 100 volts, the power used is 100 watts.

In a.-c. circuits the voltage and current are not always in phase. In fact in many circuits there is a decided difference in phase between the current and voltage. What is the power?

The power at any instant is the product of the instantaneous current and the instantaneous voltage. Thus in Fig. 85, where the voltage and the current are in phase, as in a resistance circuit, the height of the voltage line e above the horizontal, or time, axis multiplied by the height of the current line i above this axis gives the instantaneous power. This is plotted in the curve P.

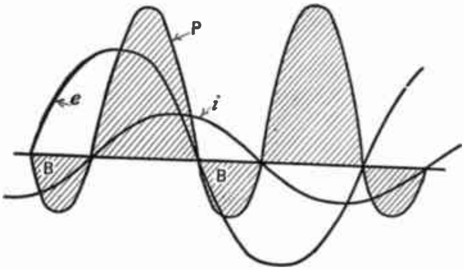


FIG. 86.—In an inductive circuit some power is consumed and some (the shaded areas below the line) is returned.

When, however, the current and voltage are not in phase, as in an inductive (Fig. 86) or capacitive (Fig. 87) circuit, a different looking curve results although the instantaneous power is still the product of the instantaneous values of current and voltage. The part of the power curve marked B is interesting. It is the result of multiplying a positive current by a negative instantaneous value of voltage. The product is negative; so the power at that instant represented by this small loop must be considered as negative power. What does this mean?

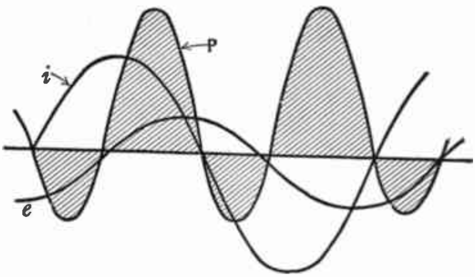


FIG. 87.—Power in a capacitive circuit.

Power consumed in a circuit is considered as positive power. Negative power is power that is returned to the generator from the line. Power is only returned to the generator when there is reactance in the circuit. A pure resistance circuit consumes the entire amount of the power fed it by the generator; a reactive circuit returns some of it to the generator.

The **effective power** in a resistance circuit is the product of the effective volts and the effective amperes. In a reactive circuit, however, the effective power is reduced by the power returned to the generator, so that the product of effective volts times effective amperes does not give the true measure of the power consumed in the circuit. The true power is given by

$$P = E_F I_F \cos \theta,$$

where θ is the angle between the voltage and the current.

The product of the volts and the amperes is called the apparent power. Since this apparent power must be multiplied by $\cos \theta$, this factor is called the power factor of the circuit. When the current and voltage are in phase, that is, in a resistance or resonant circuit, the power factor, $\cos \theta$, is equal to 1.0, and the circuit is said to have unity power factor.

wrk problems

CHAPTER VII

RESONANCE

THE most important circuits in radio are those in which either series or parallel resonance occurs. In transmitting and receiving systems resonance is used to built up large voltages and currents at certain desired frequencies and to discriminate against undesired signal frequencies by keeping their voltages and currents low. When one tunes a radio receiver, he actually adjusts the a.-c. circuits within the receiver so that a condition of resonance occurs. Everyone who has operated a receiver has, in tuning it, performed one of the most interesting experiments in all a.-c. theory and practice. It is necessary that we look into the phenomenon of resonance very closely.

110. Series resonant circuit.—Although a general idea may be obtained of what takes place in a resonant circuit when a radio receiver is tuned, a much more exact idea may be had as a result of a laboratory experiment.

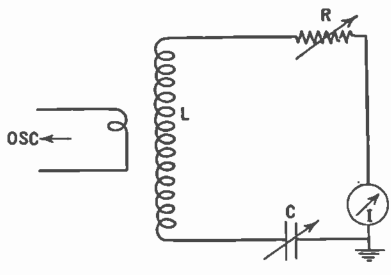


FIG. 88.—When L is coupled loosely to a generator and C is varied, the current indicated at I will go through a maximum like that in Fig. 90.

Experiment 1–7.—Connect, as in Fig. 88, a coil of about 200 microhenries inductance, a variable condenser of maximum capacity of 1000 mmfd., a resistance of about 10 ohms, and a current-indicating device such as a current squared meter or a thermocouple and meter. Couple the circuit loosely to a radio-frequency generator and (a) adjust the condenser C so that resonance is obtained and then (b) adjust the frequency of the oscillator while the tuning condenser C of the external circuit is held constant. Plot the current in the circuit against condenser degrees or capacity and then against frequency. Change the value of R and repeat.

In either case the voltage across the condenser and across the coil and the phase between current and voltage should be calculated and plotted.

NOTE.—If the experimenter possesses a short-wave transmitter which is equipped with an antenna meter he can carry out the same experiment by noting the antenna current as the antenna series condenser is adjusted, or as the frequency of the closed circuit is adjusted below and above resonance with the antenna. Such a curve is shown in Fig. 89.

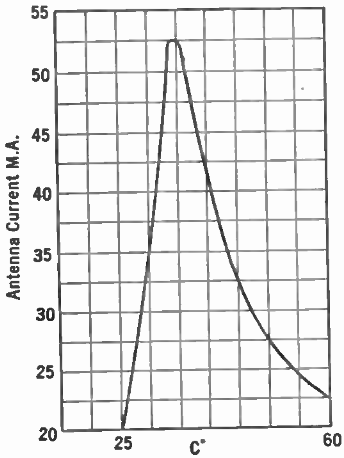


FIG. 89.—How the antenna current of a radio station varies as the series condenser is varied.

Experiment 2-7.—Connect in series with a lamp an inductance of several henrys. Add sufficient resistance so that the lamp does not light when placed across a 110-volt 60-cycle line. Then put a condenser (of the filter type) in series with the resistance, the line, and the lamp. Add other capacity until the lamp lights up. Adding the capacity has brought the circuit to resonance so that the only hindrance to the flow of current was the lamp and the resistance. Adding something to the circuit actually made more current flow.

The curve in Fig. 90 shows what happens as the voltage across a series circuit is kept constant but the frequency is increased. At first the current increases slowly, then as the resonant frequency, 356 kc., is approached the current increases very abruptly and after passing through a sharp maximum at 356 kc. falls very rapidly at first and then more slowly. The voltages across coil and condenser go through similar changes. The phase between current and voltage changes also, being a negative angle (current leading voltage) below resonance, being zero at resonance (current and voltage in phase), and becoming a positive angle above resonance (current lagging behind voltage).

At zero frequency, that is at direct-current, the current in such a circuit would be zero because the condenser will not permit d.-c. current to pass. At very low frequencies, the reactance of the condenser is very high, so that little current will flow. At very high frequencies the reactance of the coil becomes very great and therefore little current will flow. At intermediate frequencies more current flows.

When a series circuit is resonant, the current and voltage are in phase, the current is a maximum, the impedance is a minimum, the voltages across the condenser and the inductance are equal and

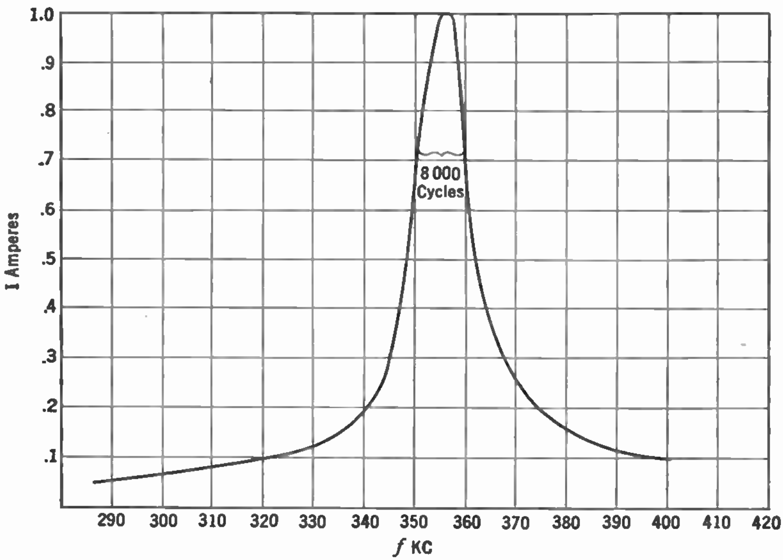


FIG. 90.—The resonance curve of a circuit like that of Fig. 89.

opposite in sign and greater in value than the voltage across the combination.

In Fig. 90 note that from 340 to 356 kc., a change of 1.047 times, the current changes from 0.19 amperes to 1.0 amperes, a change of 5.2 times. The voltages across the condenser and inductance become much greater, at resonance, then the voltage impressed upon the circuit. This voltage may become so high that the condenser will be punctured. The voltage across the coil or the condenser at resonance is equal numerically to the voltage across the entire circuit multiplied by the factor X_L/R or X_C/R which are equal to $L\omega/R$ or $1/C\omega R$.

A curve showing how the current in the circuit changes as the variable factors are changed, that is, a graph of I against the capacity, the inductance or the frequency, is called a **resonance curve** and is symmetrical about the resonant frequency if the circuit is adjusted by changing the inductance, and is dissymmetrical when the capacity or the frequency is the variable factor.

111. Characteristics of series resonant circuit.—Below the resonant frequency the reactance is mainly capacitive; above this frequency the circuit is mainly inductive. That is: the capacitive reactance is the main deterrent to the flow of current below resonance; above resonance the inductance offers the greatest opposition to the flow of current. For a narrow band of frequencies in the neighborhood of 356,000 cycles the total impedance of the circuit is less than 100 ohms. Far from the resonant frequency the reactance is much greater and very little current will flow.

Below resonance, where the capacity reactance predominates, the current leads the voltage; at resonance the current is in phase with the voltage; above resonance the current lags behind the voltage.

At all frequencies the voltage across the inductance is 90° ahead of the current and the voltage across the condenser is 90° behind the current. Between the two reactive voltages, then, is a 180° phase difference. That is, they are exactly out of phase. Their resultant may be found by looking at Fig. 91 in which E_L and E_C are plotted as 180° out of phase and of unequal magnitude. The resultant of combining them with the voltage

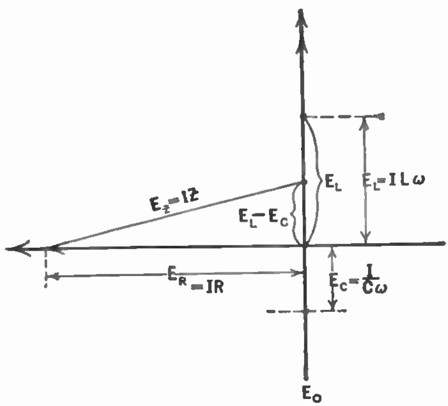


FIG. 91.—Vector diagram of a series circuit in which inductance predominates.

across the resistance must be the voltage across the entire series circuit, which is the vector sum. Thus,

$$E = \sqrt{E_R^2 + (E_L - E_C)^2}$$

At any frequency but that of resonance, one of the two reactive voltages is greater than the other. At resonance, however, the two voltages are equal in magnitude and opposite in phase so that the resultant of combining the reactive voltages is zero. When added vectorially to the IR drop in the circuit, the resultant is the voltage which is impressed by the external source.

The vector sum of the reactive and resistive voltages is equal to the impressed voltage.

Example 1–7.—What are the voltages and phase relations in the circuit of Fig. 88 at a frequency of 370 kc.?

$$I = .274 \text{ ampere}$$
$$X_C = 430 \text{ ohms}$$
$$X_L = 466 \text{ ohms}$$
$$R = 10 \text{ ohms}$$
$$E_R = I \times R = .274 \times 10 = 2.74 \text{ volts}$$
$$E_C = I \times X_C = .274 \times 430 = 118 \text{ volts}$$
$$E_L = I \times X_L = .274 \times 466 = 128 \text{ volts}$$
$$E_{R+L} = \sqrt{2.74^2 + 128^2} = 128 \text{ volts (approx.)}$$
$$\phi_{R+L} = \tan^{-1}\frac{128}{2.74} = \tan^{-1} 46.6 = 88.46°$$
$$E_{R+C} = \sqrt{2.74^2 + 118^2} = 118 \text{ volts (approx.)}$$
$$\phi_{R+C} = \tan^{-1}\frac{118}{2.74} = \tan^{-1} 43 = -88.38°$$
$$E_{L+C} = E_L - E_C = 9.6 \text{ volts} = E_X$$
$$E = I\sqrt{R^2 + X^2} = \sqrt{E_R^2 + E_X^2} = \sqrt{2.74^2 + 9.6^2}$$
$$= 10 \text{ volts}$$
$$\phi_{R+L+C} = \tan^{-1}\frac{X}{R} = \tan^{-1}\frac{X_L - X_C}{R} = \frac{466 - 430}{10} = 3.6$$
$$= 74° 30'$$

At resonance the reactances are equal to each other and equal to $\sqrt{\frac{L}{C}}$, i.e., $X_L = X_C = \sqrt{\frac{L}{C}}$.

For example the reactances of the condenser and inductance in the circuit of Fig. 88 may be found by

$$X_L = X_C = \sqrt{\frac{L}{C}}$$
$$= \sqrt{\frac{200 \times 10^{-6}}{1000 \times 10^{-12}}}$$
$$= \sqrt{.2 \times 10^6}$$
$$= \sqrt{.2} \times 10^3$$
$$= .447 \times 10^3$$
$$= 447 \text{ ohms.}$$

At resonance the inductive reactance and the capacitive reactance in the equation for the impedance $Z = \sqrt{R^2 + (L\omega - 1/C\omega)^2}$ cancel out, that is, $L\omega - 1/C\omega = 0$ so that the resultant impedance is the resistance alone,

$$Z = R \text{ (at resonance)}$$

Problem 1-7.—An inductance of .3 mh., a condenser of .0001 mfd., and a resistance of 5 ohms are in series. Across the ends of this circuit is an alternator whose frequency is 900,000 cycles and whose voltage is 5. Calculate the current flowing, the phase between the current and voltage, the voltages across the coil and the condenser. What would the current be if the circuit were resonant? What is the impedance of the circuit at 900 kc.?

112. Effect of resistance on series resonant circuit.—At resonance the magnitude of the current in the circuit is controlled solely by the resistance. Its effect is most important in any radio circuits where resonance plays a prominent part. The curves in Fig. 92 show the effect of adding various resistance to the circuit of Fig. 88. The voltages across the condenser and the inductance, too, depend upon the resistance of the circuit. They are greater the smaller the resistance. This is due to the fact that the voltage across these reactances is equal to the product of the reactance and the current. The latter, controlled entirely by the resistance at resonance, in turn produces greater voltages across the reactance when less resistance is in the circuit. If E is the voltage

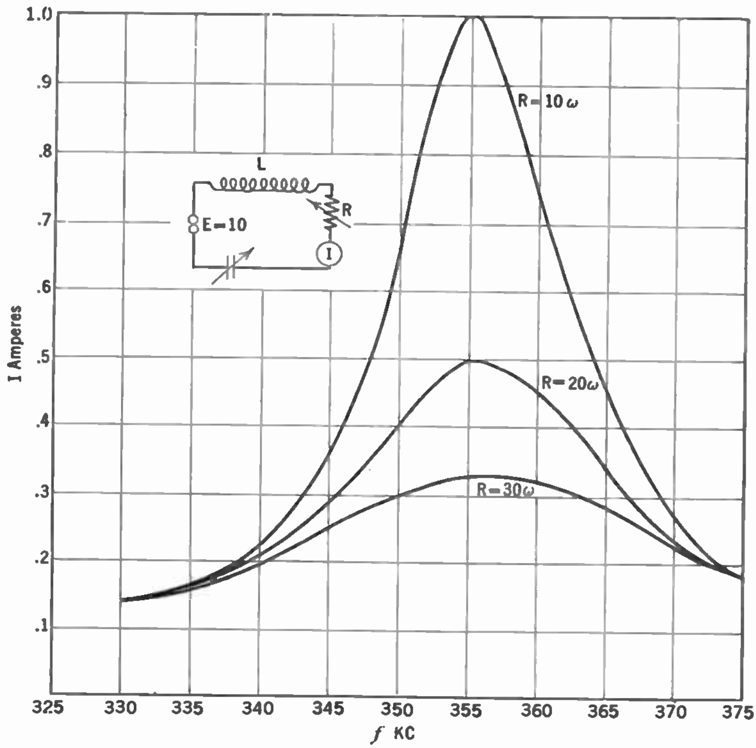


FIG. 92.—Effect of resistance on a resonance curve. Note that the current far from resonance is not changed so much as the resonant current.

impressed on the whole circuit, the voltage across the condenser is $E \div C\omega R$ and that across the inductance at resonance is $E \times \frac{L\omega}{R}$.

113. Power into resonance circuit.—No power is dissipated in heat in a pure inductance or capacity, but energy stored at one instant in a magnetic or electrostatic field is turned back into the circuit at another instant. Power is expended in the resistance of a circuit, but since at high values of resistance the current is small, the power in the circuit will be small. This power is equal, as usual, to

$$P = I^2 \times R$$

where R is the resistance of the circuit. In case of Fig. 88, where the resistance is 10 ohms and the current at resonance 1 ampere, the power is 10 watts. Since at resonance there is no reactance effective in the circuit the power fed into it by the generator is the product of the current times the voltage, or 10×1 or 10 watts.

In other words, all the energy taken from the generator is used up in heating the resistance. None is necessary to maintain the magnetic and electrostatic fields of the coil and the condenser. The energy in these fields is transferred from one to the other, the sum at any one instant being equal to the sum at any other instant so long as the energy dissipated in the resistance is supplied from the outside.

Problem 2-7. What power is taken from the generator in Problem 1-7?

In actual circuits the resistance is not isolated as in our demonstration problems. All coils have resistance; so do all condensers, although the resistance of modern variable capacities is quite small. These resistances take power from the generator and reduce the maximum height of the resonance curve.

114. The resonant frequency of the circuit.—The condition for series resonance—that the reactances of the circuit add up to zero—is fulfilled when

$$X_L = X_C$$

or

$$X_L - X_C = 0$$

or

$$\omega L - \frac{1}{C\omega} = 0$$

or

$$\omega L = \frac{1}{\omega C}$$

or

$$\omega^2 = \frac{1}{LC}$$

and since $6.28 \times f = \omega$,

$$f = \frac{1}{6.28\sqrt{LC}},$$

and since 6.28 is equal to the mathematical expression 2π we arrive at the familiar expression for the resonant frequency of a circuit as

$$f = \frac{1}{2\pi\sqrt{LC}}$$

in which f = the frequency in cycles;
L = the inductance in henrys;
C = the capacity in farads;
π = the Greek letter " Pi " and is equal to 3.1416 . . . .

Example 2–7. To what frequency will a circuit tune which has an inductance of 0.25 henry and capacity of 0.001 mfd.?

Let us write the above formula as

$$f^2 = \frac{1}{4\,\pi^2\,LC} = \frac{1}{39.5\,LC}$$

$$f^2 = \frac{1}{39.5 \times .25 \times .001 \times 10^{-6}}$$

$$= \frac{10^9}{39.5 \times .25}$$

$$= \frac{10^9}{9.87}$$

$$f = \sqrt{101} \times \sqrt{10^6}$$

$$= 10.1 \times 10^3 \text{ cycles}$$

$$= 10.1 \text{ kc.}$$

Such an expression for the resonant frequency of a circuit shows that the frequency depends upon the product of L and C, and not upon either of them alone. If L is doubled, C can still be halved and the natural frequency of the circuit will not be changed.

115. Wavelength.—The relation between the frequency of a circuit and the wavelength of transmissions to which it responds is a simple one. The **wavelength** is equal to the speed at which the electric waves travel divided by the frequency in cycles. This speed is 186,000 (approximately) miles a second and if we want the wavelength in miles we need only divide this quantity by the frequency. Ordinarily, however, we express wavelengths in meters; so it is necessary to use the velocity of transmission in meters. This is 300×10^6 meters a second, and so

$$\text{wavelength in meters} = \frac{300 \times 10^6}{f \text{ in cycles}} \quad \text{or} \quad \frac{300 \times 10^3}{f \text{ in kilocycles}}.$$

or

$$= 300 \times 10^3 \times 2\pi\sqrt{LC}$$

The customary symbol for wavelength in meters is the Greek letter "Lambda"; so the above expression may be written:

$$\lambda = \frac{300 \times 10^3}{\text{kilocycles}} = 1.884\sqrt{LC},$$

where $L = \text{microhenry} = 10^{-6}\ H$

$C = \text{mmfd.} = 10^{-12}\ F.$

Example 3–7. What wavelength corresponds to 1000 kilocycles?

$$\lambda \text{ meters} = \frac{300 \times 10^3}{1000}$$

$$= \frac{3 \times 10^5}{10^3} = 300$$

Figure 93 is a graphical method of correlating L, C, and meters of wavelength. Such a curve is called in England an "abac." A table of "LC" products will be found inside of rear cover.

Problem 3–7. What inductance must be placed in series with a 2-mfd. condenser to resonate at 60 cycles? If the voltage across the combination is 110 (effective) and the resistances in the coil and condenser add up to 20 ohms, what power is consumed in the circuit at resonance, what is the resonant current, and what voltage then appears across condenser and inductance?

Problem 4–7. A coil of 0.15 henry is in series with a condenser of 28.5 mfd. and a resistance of 5.8 ohms. The voltage across the circuit is 22 volts, the frequency is the resonant frequency of 80 cycles. What would the voltage across the condenser be if the resistance were doubled? What power is being wasted in heat at resonance?

Problem 5–7. A variable condenser has a range from maximum to minimum capacity of 9 to 1, that is, from 0.0005 to 0.0000555 mfd. What wave-length range will it cover with a given coil, that is, what is the ratio between the longest and shortest wave to which it will tune the coil?

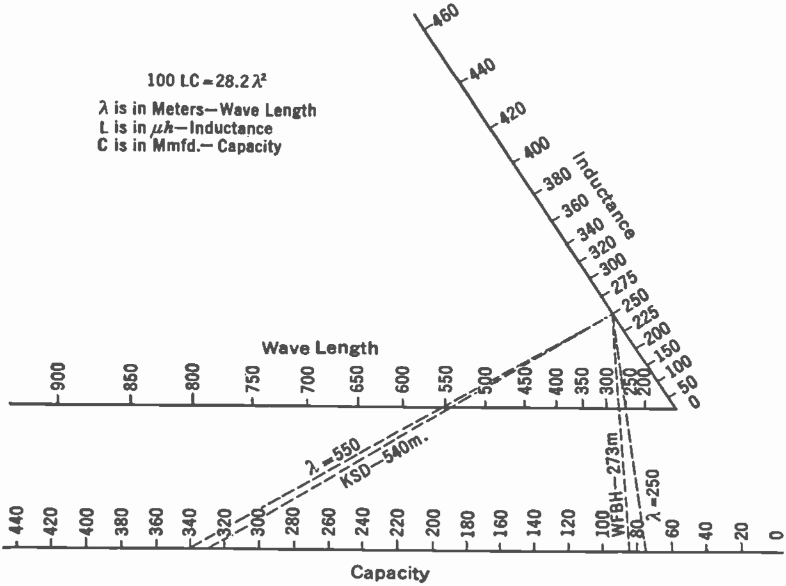


FIG. 93.—Drawing a straight line through two points (L and λ for example) and intersecting the third line gives the unknown quantity desired (C).

Problem 6–7. In Problem 1–7 what would happen to the voltage across the condenser if the capacity were reduced to half, resonance being maintained by other means which also keep the original current?

Problem 7–7. An antenna may be represented by an inductance of 50 microhenrys in series with 0.00025 mfd. capacity and 30 ohms resistance. What is its resonant frequency? If a distant station transmitting on this frequency produces a voltage of 1000 microvolts across the ends of this antenna system, what current will flow? What will be the ratio of currents at the resonant frequency to signals of equal voltage at the antenna but differing from the resonant frequency by 50 kc., say 50 kc. above resonance? What is the resonant wavelength of the antenna?

Problem 8–7. It is desired to make a receiving set able to receive signals from 800-meter stations. At present the maximum wavelength that can be received is 600 meters. The tuning condensers have a maximum capacity of 500 mmfd. What capacity must be added in parallel to the present tuning condenser to enable the 800-meter signal to be heard?

Problem 9–7. What can be done to increase the current at 150 meters in the antenna of Problem 7–7? Suppose another 50-microhenry coil is placed in series with the antenna. What must be done to bring the circuit to resonance with the 150-meter signals? At resonance, what voltage will appear across the 50-microhenry inductance, if $C = 0.000126$ mfd. and $R = 30$ ohms?

Problem 10–7. What power is being lost in this antenna at resonance?

Problem 11–7. The primary of a good audio-frequency choke coil has 100 henrys inductance. In many circuits a condenser is placed across the primary so that high radio frequencies will not have to pass through the transformer. If this condenser has a capacity of 0.001 mfd., what is the decrease in effective impedance of the circuit to a frequency of 10,000 cycles?

Problem 12–7. A loud speaker is often coupled to a power tube through a condenser as in Fig. 94. If the speaker has an inductance of one henry and the condenser is a 4-mfd. unit, to what frequency will the combination become resonant?

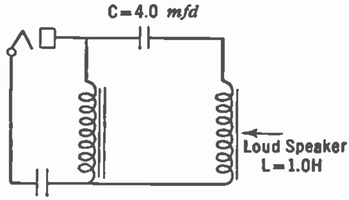


Fig. 94.—To what frequency will the loud speaker and condenser tune?

Problem 13–7. Plot a curve of the reactance of the loud speaker in Problem 12-7 from 100 to 10,000 cycles.

Problem 14–7. In an amateur's short-wave transmitting station a 100-mmfd. condenser is in series with the antenna. What voltage has this condenser across it, if the wavelength is 30 meters and the antenna current is one ampere?

Problem 15–7. In a similar transmitting circuit an amplifier is used to boost the output of an oscillator before being fed into the antenna. The grid of this amplifier's tube requires a voltage of 80 volts at 40 meters (7500 kc.). This voltage is to be obtained across an inductance of 4.5 microhenrys. How much current must flow through the inductance? What capacity must be across it if the coil and condenser are to tune to 40 meters?

116. Parallel resonance.—Many of the circuits used in radio involve resonance in a branched or parallel circuit. Figure 95 shows a typical parallel circuit composed of an inductance shunted by a condenser, the combination forming what is sometimes called an " anti-resonant " circuit. The effects of varying the frequency of the voltage across the circuit are widely different from the effects in a series circuit. In the latter, the currents become very large at resonance and the resultant series impedance of the circuit becomes small. In the parallel case the circuit offers a large impedance to the generator and the current becomes very small. In the series case the same current flows through the condenser and the coil. The voltages across these units differ. In the parallel case the same voltage is across each branch, but the currents through them differ.

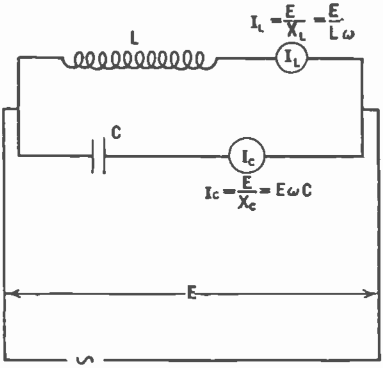


FIG. 95.—An anti-resonant circuit.

Experiment 3-7. Connect as in Fig. 95 the coil and condenser used in Experiment 1-7. If sufficient meters are available read the a.-c. current in the two branches as well as the current from the generator as the frequency of the generator is changed. Then fix the generator frequency and adjust the condenser capacity until maximum resonance occurs. Plot the currents against frequency and against condenser capacity. The generator in this experiment may be a small oscillating tube. A 5-watt output is sufficient to produce currents in the branches of the circuit of 100 milliamperes which can be read with a Weston Model 425 thermo-galvanometer.

In case laboratory apparatus is not available, the current may be calculated after L, C, and E values have been chosen.

The same voltage exists across the branches and the circuit as a whole. The current taken by each branch is the ratio between the voltage and the reactance of that branch. Thus,

$$I_L = \frac{E}{X_L} = \frac{E}{L\omega}$$

$$I_C = E/X_C = EC\omega$$

$$I = I_L - I_C = E\left(\frac{1}{L\omega} - C\omega\right) = E\left(\frac{1 - CL\omega^2}{L\omega}\right).$$

As the frequency is increased, more and more current is taken by the capacity branch, less and less by the inductance branch. In the series case the voltages across coil and condenser are out of phase; their algebraic sum at any frequency combined vectorially with the IR drop is the voltage across the combination. In the parallel case the currents are out of phase; at any frequency their algebraic sum combined vectorially with the shunt resistance current (if any) give the current taken from the generator. In the simple case where the resistance is neglected, the algebraic sum of the currents gives the generator current. Since these two currents are out of phase (the capacity current has a negative sign), adding them algebraically actually means subtracting I_C from I_L.

At resonance the currents taken by the two branches are equal and if there is no resistance in the circuit the current taken from the generator is zero, because it is the difference of the two branch currents which is read in the generator circuit ammeter.

The impedance of the circuit as a whole, that is, the impedance into which the generator must feed current, is the ratio between the voltage and current as usual:

$$Z = E/I.$$

Therefore, if no current flows, the circuit has infinite impedance. Actually there is always some resistance in the circuit. This may be in an additional shunt path, or it may exist in one or both of the other branches. Actually, then, the generator current does not fall to zero but passes through a minimum value. In most radio circuits by far the greater part of the resistance which is in the circuit resides in the coil since the resistance of the average well constructed condenser used at radio frequencies is very small. In such a circuit in which there is resistance in series with the inductance and which is tuned to resonance by varying the value of the capacity, C, the condition for resonance (minimum current from the generator) is:

$$C\omega = \frac{L\omega}{R^2 + L^2\omega^2}$$

The current taken by the circuit is not exactly in phase with the generator voltage and so minimum-current resonance differs slightly from zero-reactance resonance.

$$I_r = \frac{ER}{R^2 + \omega^2 L^2}$$

and the impedance presented to the generator is

$$= \frac{E}{I_r} = \frac{R^2 + \omega^2 L^2}{R}.$$

117. Effective resistance.—If, as is usual, the resistance of the coil is small compared to its reactance, the condition for resonance is

$$\omega C = \frac{1}{\omega L}$$

and the minimum current from the generator becomes

$$I_r = \frac{ER}{\omega^2 L^2},$$

and since the impedance of the circuit is equal to the ratio between the voltage across it and the current through it, it becomes

$$= \frac{\omega^2 L^2}{R} = \frac{L}{CR}.$$

Since at resonance the current into the circuit from the generator is in phase with the voltage, E, across the circuit, the expression above is not a true impedance but is more nearly a resistance. It may be called the " effective resistance " of the circuit.

118. Resonant frequency.—In this manner we arrive at the frequency to which a low resistance circuit becomes resonant:

$$\omega C = \frac{1}{L\omega}$$

$$f = \frac{1}{2\pi\sqrt{LC}}.$$

The condition for resonance then is that the inductive and capacitive reactances are equal but opposite in sign—which is the same condition that holds for series resonance. Here, however, there are other conditions. The resistance must reside in the coil and must be small compared to the reactance of the coil.

For example, in the case of the circuit in Fig. 95:

$$L = 200\ \mu H$$
$$\omega = 2\pi \times 356{,}000$$
$$R = 10 \text{ ohms (in the coil)}$$
$$X_L = L\omega = 200 \times 10^{-6} \times 2\pi \times 356{,}000$$
$$= 447 \text{ ohms.}$$

Here we may neglect the effect of resistance and use the simple relation for resonant current and for impedance.

If $$E = 10$$

$$I = \frac{ER}{\omega^2 L^2} = \frac{ER}{(X_L)^2}$$

$$= \frac{10 \times 10}{447^2}$$

$$= .5 \times 10^{-3} \text{ amps.} = \tfrac{1}{2} \text{ milliampere}$$

and $$= \frac{\omega^2 L^2}{R} = \frac{447^2}{10} = 20{,}000 \text{ ohms.}$$

At frequencies other than resonance the impedance is $\dfrac{L\omega}{1 - CL\omega^2}$ provided there is no resistance in the circuit.

At lower frequencies than resonance most current goes through the inductance because its reactance is low whereas that of the condenser is high. As the reactance of the condenser decreases, with increasing frequency, and that of the inductance increases, and since the generator current is the actual difference between these currents, the generator current decreases as resonance is approached. At low frequencies the circuit is said to be inductive and at high frequencies is capacitive.

119. Uses of series and parallel resonant circuits.—Whenever it is desired to secure a large current and a low impedance circuit, series resonance is utilized. When it is desired to built up a high impedance or a high voltage circuit an anti-resonant circuit is used. Let us consider the antenna-ground system in Fig. 96. The antenna has in series with it an inductance across which a voltage is to be developed at a desired frequency. In series with this inductance are a capacity for tuning purposes and an anti-resonant circuit. Voltages of various frequencies, among them the desired frequency, are impressed on the antenna by distant transmitting stations. The maximum voltage is desired across the inductance, *L*, at the desired frequency and the minimum at other frequencies. There is a specially strong signal which is setting up a voltage across the antenna. The anti-resonant circuit is tuned to this frequency.

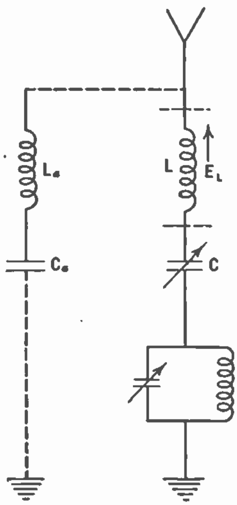


Fig. 96.—The anti-resonant circuit in series with the antenna rejects undesired signals by making the series impedance to them very high.

The condenser *C* is adjusted until the antenna system as a whole is resonant to the desired signal. A large current flows through the series system, building up a large voltage across *L*. Voltages of other frequencies cause small currents to flow in the antenna system and consequently small voltages at these frequencies are built up across the coupling coil, *L*. The anti-resonant circuit's being tuned to the unwanted signal makes the antenna system as a whole have a very high impedance at this frequency and so very small currents will flow through it, building up small voltages of this frequency across the coupling coil.

Such an anti-resonant circuit is often called a **rejector** circuit because it rejects signals of the frequency to which it is tuned.

The series resonant circuit is called an **acceptor** because it accepts signals of the resonant frequency. The rejector used in this circuit is commonly known as a **wave trap** because it traps out unwanted signals.

Let us suppose signals are fed into the input of an amplifier which has an internal resistance, R, which is in series with an output circuit, as shown in Fig. 97. The voltage across this output, Z, is to be made as high as possible. The amplifier has available a certain voltage, E, which must be divided between the internal resistance of the amplifier and the output load. The proportion of the voltage that appears across this load increases as its ohmic

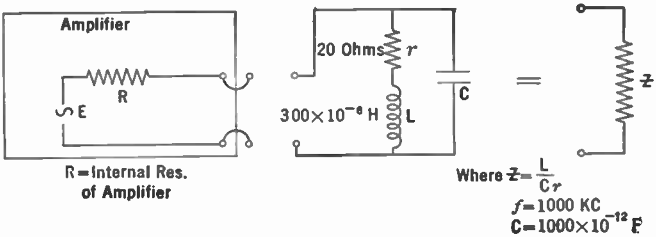


FIG. 97.—A high impedance is desired for the amplifier to work into. A tuned circuit does the trick. Numerically it is equal to Z.

impedance increases with respect to the amplifier's resistance. Thus, if the output impedance is equal to the internal resistance of the amplifier, one-half of the total voltage available will appear across it. If it is higher than this value, a greater proportion of voltage will be usefully applied across the load and less used up in the resistance.

In this case the anti-resonant circuit is used. At resonance its impedance becomes equal to $\dfrac{L}{CR}$ or $\dfrac{L^2\omega^2}{R}$

$$= \frac{(300 \times 10^{-6})^2 \times (6.28 \times 1000 \times 1000)^2}{20}$$

$$= 180{,}000 \text{ ohms.}$$

If the amplifier's internal resistance is equal to 20,000 ohms, the voltage across the tuned circuit is $\frac{180}{200}$ or $\frac{9}{10}$ of the total available voltage.

Problem 16–7. A screen-grid tube gives the greatest voltage amplification when worked into a very high impedance. A condenser of 1500 mmfd. is available. Calculating the size of the inductance required to tune to 1000 meters and assuming it has a resistance of 30 ohms, what is the impedance $\left(\frac{L^2\omega^2}{r}\right)$ that can be presented to the tube by shunting the coil and condenser?

Problem 17–7. A wave trap is to be put into an antenna and tuned to a station whose frequency is 750 kc. What will be a convenient size of condenser and coil to use? They are to be shunted across each other and the combination put in series with the antenna. If the coil has a resistance of 10 ohms and the condenser a resistance of 1.0 ohm at this frequency, what impedance will the trap offer to the offending signal?

Problem 18–7. In Problem 17–7, neglecting phase differences between the trap and the rest of the antenna, if the total impedance of the antenna to the offending signal is double that of the trap alone so that one-half of the total antenna voltage is across the trap, what current will flow through the condenser if the total 750-kc. voltage across the system is 10 microvolts?

120. Sharpness of resonance.—The effect of resistance is to reduce the maximum current flowing in a series resonant circuit, and to make less pronounced the minimum of current flowing into a parallel resonant circuit from an external source.

Since the maximum current is desired in a series circuit, and the maximum impedance in a parallel case, the inclusion of resistance in either is deleterious.

Let us consider the antenna illustrated in Fig. 96. Suppose its inductance, L, is 200 microhenrys and C at resonance (356 kc.) is 1000 mmfd. For the moment we shall neglect the presence of the wave trap. Assume a voltage of 10 volts. What is the effect on the resonance curve of this antenna system if it has a resistance of 10 ohms or of 40 ohms? The current at resonance in the 10-ohm case is 1 ampere whereas at 370 kc. the current is .274 ampere, a ratio of 3.65. In this 40-ohm case, the resonant current would be only 0.25 ampere—one-fourth of its value with the lower resistance—and the current at 370 kc., i.e., 14 kc. off resonance, would be .188 ampere. This is a current ratio between the resonant and the off-resonant current of only 1.33.

In other words, if the antenna had impressed on it from equally distant and equally powerful radio stations two voltages, one of 356 kc.—the desired frequency,—and one of 370 kc.—the unwanted frequency,— 3.65 times as much current flows at the desired frequency as the unwanted. In the 40-ohm antenna, however, not only is the desired current cut to one-quarter of its other value but the ratio of wanted to unwanted current has been decreased to 1.33. The low-resistance antenna is said to be more " selective " and its " selectivity " is decreased when resistance is added to it.

121. Selectivity.—The selectivity of a circuit is a measure of its ability to distinguish between wanted and unwanted signals. The steepness of the resonance curve is a direct measure of this selectivity.

Let us consider the parallel or anti-resonant circuit. At its resonant frequency it keeps currents of undesired frequency from flowing through the antenna because of its high impedance at those currents. This impedance, $L^2\omega^2/r$, increases as the resistance of the circuit decreases, so it behooves the designer to use low-resistance coils and condensers when building a trap or rejector circuit.

Since a circuit may be tuned to resonance by varying any one of three variable factors, the inductance, capacity, or frequency, we may express the sharpness of resonance in any one of three ways. It may be the fractional change in current for a given fractional change in either L or C. Naturally the sharper the resonance curve and the greater its height, the greater will be the current change for a small number of degrees of change in the tuning condenser. The circuit will tune " sharply "; it is called a sharp circuit. In practice the condenser is used as the tuning variable. If, then, the current at resonance I_r and the tuning capacity C_r are noted and then changed to give some other value of current, the sharpness of resonance may be found by substituting values in the following expression,

$$S_{res} = \frac{\sqrt{\dfrac{I_r^2 - I^2}{I^2}}}{\dfrac{C_r - C}{C}}.$$

By some mathematical juggling of this cumbersome expression (see Bulletin 74, Bureau of Standards, page 36) a much simpler expression may be obtained. This has two forms,

$$\text{Sharpness of resonance} = \frac{1}{R\omega C_r} = \frac{L\omega}{R},$$

where R = the resistance of the circuit;

C_r = the capacity at resonance;

L = the inductance of the circuit.

In other words the sharpness of resonance is the ratio between the capacitive or inductive reactance to the resistance, and thus the resonance curve rises the steeper the less resistance there is in the circuit.

Another expression for the sharpness of resonance is obtained by varying the frequency and noting how the current changes. Thus an expression is worked out which shows the width of the resonance curve where the current is equal to $.707 \times I_r$, where I_r is the resonant current.

Suppose, as in Fig. 98, we plot a resonance curve of current against capacity. Suppose the capacity is adjusted until the total reactance in the circuit $(X_L - X_C)$ is equal to the resistance in the circuit. That is,

$$(X_L - X_C) = R,$$

when $$I = \frac{E}{\sqrt{R^2 + X^2}} \text{ becomes equal to } \frac{E}{\sqrt{2\,R^2}}$$

and $$I = .707\,I_r$$

then $$\frac{L\omega}{R} = \frac{2\,C_r}{C_2 - C_1},$$

in which C_r = the capacity at resonance;

C_1 and C_2 = the two values of capacity which makes $I = .707\,I_r$.

122. Width of resonance curve.—If, however, the frequency of the impressed voltage is so adjusted that two currents are reached, above and below the resonant frequency f_r, which are equal to .707 I_r,

$$\frac{L\omega}{R} = \frac{fr}{f_2 - f_1},$$

whence the width of the frequency band

$$f_2 - f_1 = \frac{Rfr}{L\omega} = \frac{R}{2\pi L}$$

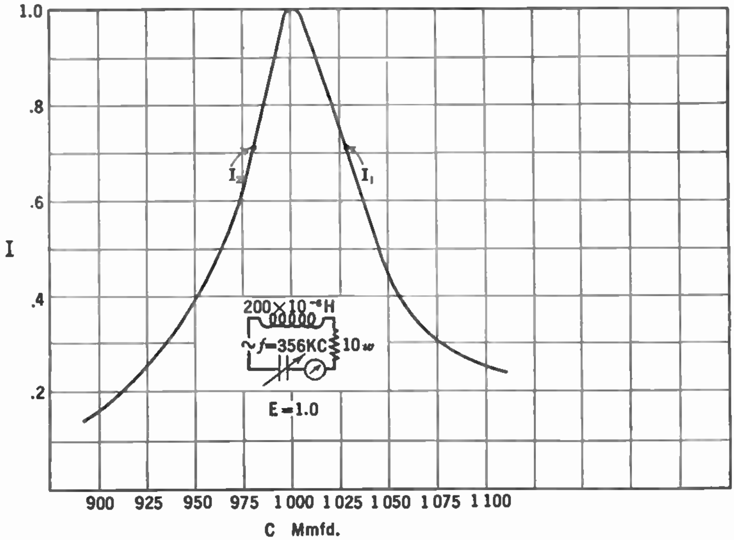


FIG. 98.—If I_1, and I_2 are equal to 0.707 times the resonant or maximum current, the resistance of the circuit may be calculated.

Example 4–7. What will be the width in cycles of the resonance curve at a point where $I = .707\ I_r$ when $L = 200\mu h$, $R = 10$ ohms, $f = 356{,}000$ cycles?

$$f_2 - f_1 = \frac{10 \times 356{,}000}{447} = \frac{R \times fr}{L\omega}$$

$$= 8000 \text{ cycles}$$

and if

$$\frac{L\omega}{R} = \frac{2\,C_r}{C_2 - C_1}$$

$$C_2 - C_1 = \frac{2\,C_r \times R}{L\omega}$$

$$= \frac{2000 \times 10}{447}$$

$$= 44.7 \text{ mmfd.}$$

= change in capacity required to change the current from $I = .707\ I_r$ below resonance, to $I = .707\ I_r$ above resonance, or from I_1 to I_2 in Fig. 98.

Problem 19–7. In Fig. 98, suppose the resistance is 20 ohms instead of 10. Calculate the width of the band at the point where the current is 0.7 of its maximum value, and the change in capacity required to produce this change in current.

Problem 20–7. A certain coil-condenser combination has a resistance of 16 ohms at 400 meters. The inductance is 170 microhenrys. What is the width of band passed at the point where the current is equal to 0.7 of its maximum value? What is the discrimination between the resonance current and another current 10 kc. off resonance? What is the " sharpness of resonance " of this circuit?

Problem 21–7. A circuit is to pass only 0.707 of its maximum current at a point 2.0 kc. off resonance, which occurs at 500 kc. The condenser to be used has a capacity of 0.0006 mfd. Calculate the maximum resistance the circuit can have.

Problem 22–7. Suppose that increasing the size of an inductance by a factor of 2.0 increases the resistance in a circuit by a factor of 1.5. The circuit is to tune to the same wavelength. What has happened to the sharpness of resonance, or, what amounts to the same thing, to the selectivity of the circuit?

Problem 23–7. If the expression $L\omega/r$ of a coil remains constant over a fairly wide band of frequencies, does the selectivity of a tuned circuit differ at different frequencies? Does the width of band passed differ at 1500 kc. from what it is at 500 kc.?

The selectivity of a radio receiver can be illustrated by Fig. 188 which shows the relative gain of a stage of a radio frequency amplifier when the signal is so-and-so-many kilocycles away from the frequency to which the receiver is tuned. Note the sharpness of the curve at 550 kc. and the poor selectivity at high frequencies.

123. Effect of inductance and capacity on sharpness of resonance.—Since the sharpness of resonance expression, $L\omega/R$ and $1/\omega CR$ both show that the inclusion of resistance tends to cut down the selectivity of the circuit in which the resistance exists, it behooves the experimenter and engineer to keep the resistance of his circuits at a minimum—when selectivity is his goal. What effect has changing the ratio of inductance to capacity, the product of $L \times C$ remaining constant?

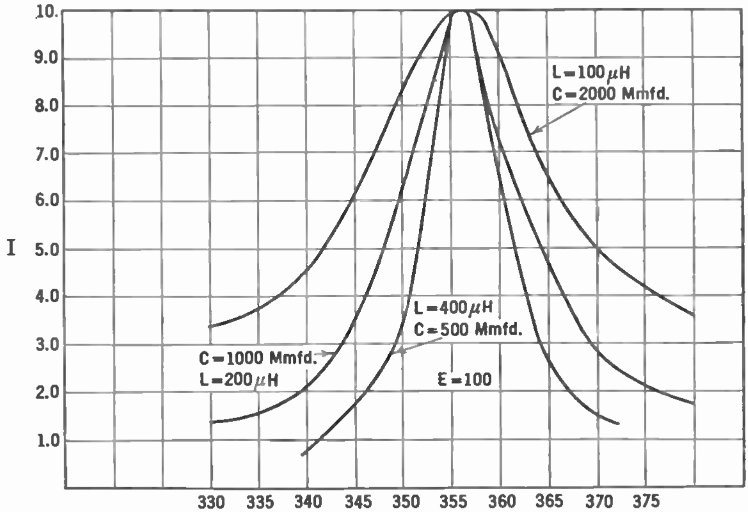


FIG. 99.—Effect on sharpness of resonance of varying ratio of L to C.

Let us consider the ratio of inductive reactance or resistance, $L\omega/R$. If we can increase L without increasing R we shall increase the sharpness of resonance. Now considering the ratio of capacitive reactance to resistance, $1/C\omega R$, increasing C has the same effect as increasing the resistance—the sharpness of resonance is decreased, the selectivity of the circuit goes down.

In a series circuit, then, the selectivity increases as the ratio L/C increases. Some theoretical curves showing this effect are plotted in Fig. 99 showing that for selective circuits a large inductance and small condenser should be used. (R = 10 ohms.)

In a shunt circuit the opposite is true, the selectivity increases as the ratio of L/C decreases. In other words, for a selective parallel tuned circuit, a large capacity and small inductance should be used. Some curves showing this effect are shown in Fig. 100.

In both of these cases, the product of $L \times C$ must be a constant in order that the same resonant frequency be maintained.

124. The resistance of coils.—The difficulty with the adjustment of one's circuits to the desired selectivity by using large coils

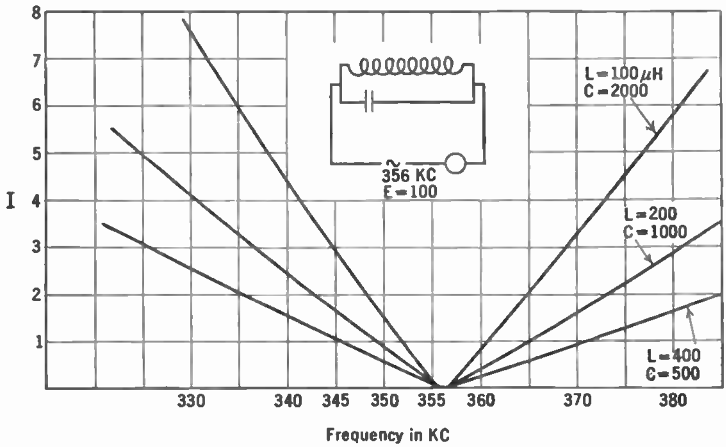


FIG. 100.—How varying $\frac{L}{C}$ affects sharpness of tuning of an anti-resonant circuit.

and small condensers or vice versa according to the above section lies in the fact that the resistance of a coil increases as the inductance is increased and the curves in Figs. 99 and 100 were plotted on the assumption that the resistance of the circuits in question remained constant. Such is not the case, and so the increase in sharpness of resonance by using a large ratio of inductance to capacity (in a series circuit) is not so pronounced as theory would indicate.

The question naturally arises, is the resistance of a coil different at different frequencies, and if so, why?

The answer is that the resistance of a coil of wire to high-frequency currents may be several times its resistance to d.-c. currents. The 200-microhenry coil used in examples several times in this chapter which at 356 kc. has a resistance of 10 ohms is a good coil, and yet its resistance to direct current is probably an ohm or less.

125. High-frequency resistance.—In all alternating current problems the resistance that is considered is the resistance at the frequency under consideration. Thus at broadcast frequencies 550 to 1500 kc., a coil will have a certain a.-c. resistance; at 60 cycles its resistance will be different, and to d.-c. currents its resistance may be still another figure.

A wire stretched out straight will have one resistance to d.-c. and another to a high-frequency current; therefore the fact that the wire is coiled up in an inductance is not the cause of the additional resistance. The difference arises from the fact that the current in a conductor at high frequencies is not evenly distributed throughout the cross-section of that conductor. Because of the rapid change of direction of flow and because the current within the cross-section of a conductor changes rapidly, small e.m.f.'s are generated in that cross-section, and therefore all along the wire. These voltages are in such a direction, according to Lenz's law (Section 55), that of the total current flowing more is along the surface of the wire and less along the inner parts of the wire. The result is a decrease in effective area of conductor and a consequent rise in resistance.

A table is given in Circular 74 (Bureau of Standards) showing the effect of diameter of wire, frequency, resistance, etc., upon this phenomenon known as "skin effect." For our purposes it is sufficient to know that the resistance of a coil to high-frequency current is always greater than its resistance to a direct current.

The resistance of a coil over the range of frequencies at which it is used changes somewhat, increasing with increase in frequency.

The manner in which the expression $L\omega/R$ of a coil, sometimes called its "Q," varies over the frequency range is plotted in Fig. 101. Knowing this factor for the coil in a series or shunt circuit we can calculate the width of the frequency band at a point where the current is 0.707 of its resonant value, we can plot a resonance curve, and can calculate the equivalent impedance of the circuit at resonance to a generator which must feed current into it.

Let us, however, measure the resistance of the coil at higher and higher frequencies. What happens? Figure 102 shows that at higher frequencies the coil resistance becomes very high and finally the curve rises perpendicularly, indicating that at some nearby point the resistance is infinite. What is happening?

126. Distributed capacity of coils.—Whenever two objects which conduct current are insulated from each other, they form a condenser. Electricity may be stored in it. Its capacity depends

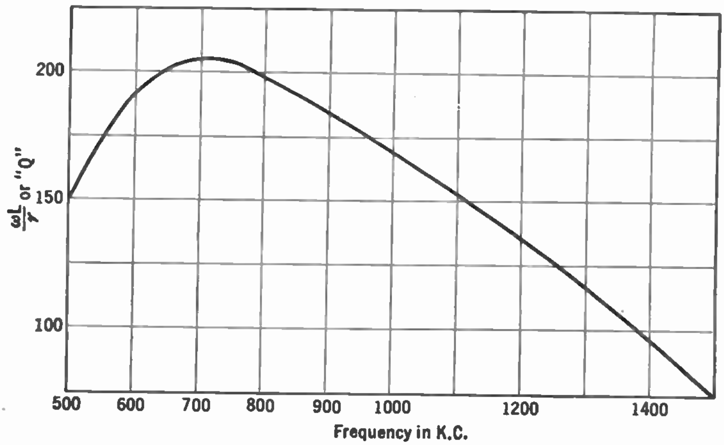


Fig. 101.—How the "Q" ($L\omega/r$) of a coil varies with frequency.

upon the proximity of the objects, the insulation between them, and their shape. In a coil of wire each turn is at a different potential from its neighbor, and is separated from it by the insulation of the wire. Thus every coil is not a pure inductance but may be thought of as a coil shunted by a capacity made up of the resultant capacity of a number of smaller capacities. At some frequency the coil shunted by its capacity becomes anti-resonant, and the circuit then becomes as shown in Fig. 103 where the tuning condenser is no longer in series with a coil but with a parallel tuned circuit which at the resonant frequency has a very high impedance. The series impedance of the circuit, then, increases as we approach the resonant frequency (sometimes called the natural wavelength or

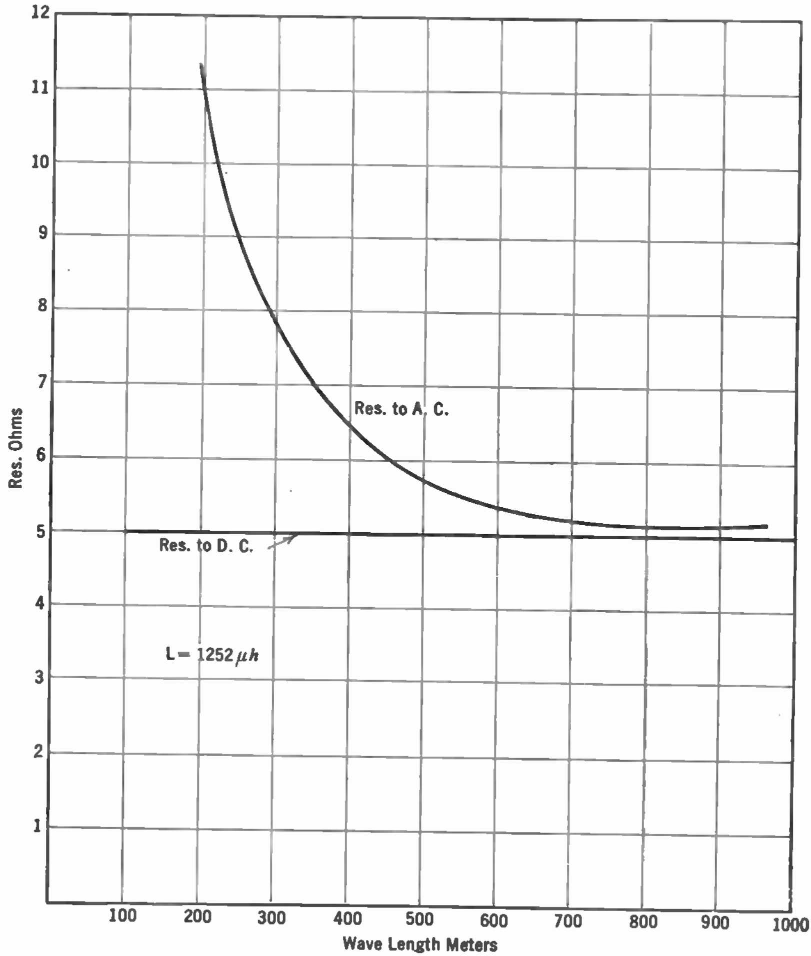


Fig. 102.—High-frequency resistance of a coil.

frequency) of the coil, and for this reason its effective resistance becomes great.

This capacity of the inductance is known as a **distributed capacity** since it is not concentrated in any one place or form but is more or less evenly distributed along the whole length of the inductance. Its effect is to lower the effective inductance of the coil and to increase its resistance somewhat. The capacity and inductance of a coil do not change much with frequency, but the apparent inductance of this anti-resonant circuit does change with frequency. It is equal to

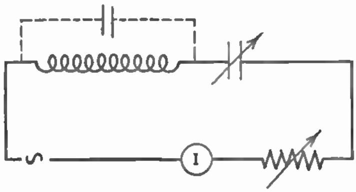


FIG. 103.—When the dotted capacity across the coil tunes it to the frequency of the generator, the series impedance of the circuit becomes very high.

$$L_a = \frac{L}{1 - \omega^2 C_o L},$$

in which C_o = the capacity of the coil;

L_a = its apparent inductance;

L = its true or low frequency inductance;

$\omega = 6.28 \times f$.

CHAPTER VIII

PROPERTIES OF COILS AND CONDENSERS

Coils and condensers form the nucleus of every radio circuit. Other apparatus is needed, of course, but for each of the other units needed there are several substitutes. There are no substitutes for coils and condensers. To understand what their rôle is in the reception of radio messages, either in code or voice or musical form, we must look at a simple receiving system.

127. Tuning a receiver.—A simple receiving circuit consists of an antenna-ground system connected to a coil and a " detector " such as a crystal of carborundum or galena or silicon or other sensitive mineral which has the property of separating the audio tones from a radio wave. A pair of head phones may be put in series with the detector so that the audio tones which are filtered out of the radio wave by the detector may be made audible. A small condenser across the phones will pass the radio frequencies but not the audio frequencies which must go through the phones.

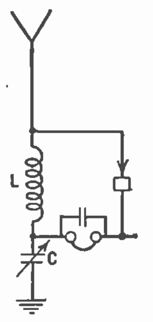


Fig. 104.—A simple radio receiver.

One way to get louder signals is to tune the antenna-ground system to the frequency of the desired wave. This is done by varying *C* in Fig. 104. When the circuit is series resonant, a large current flows through the inductance. The voltage across it ($X_L \times I$) will be large and the response from the crystal will be greater.

The voltage across the inductance can be amplified and then impressed across the detector. This amplification may take place in several stages so that very weak signals may finally be heard with the strength of nearby strong signals which are detected directly from the antenna inductance. If desired, the signals may be amplified again after detection by means of audio-frequency amplifiers.

As we have already seen (Section 121), there is another advantage of tuning the antenna, the advantage of selectivity. Signals of low frequency find considerable impedance in the condenser of such a series-tuned antenna, signals of high frequency find impedance in the coil; signals of the desired or resonant frequency find a minimum of impedance, and so the filtering action of the tuned system is advantageous. If, in addition to the series tuned circuit, we used an anti-resonant or parallel-tuned circuit as in Fig. 105, we impose more hardships upon unwanted signals. In this case when maximum current flows through L_1 maximum current is induced in L_2. If, then, C_2 is tuned so that L_2C_2 form an anti-resonant circuit, the impedance to the resonant frequency will be very high and any current through it will build up a large voltage across it so that the detector gets a high voltage at the desired frequency and a low one at all other frequencies—and the selectivity of the system as a whole is improved.

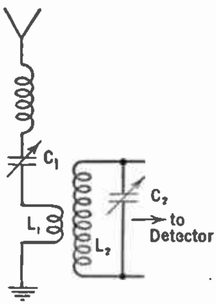


FIG. 105.—Varying C_1 until the antenna system as a whole is series resonant increases voltage across L_1.

If, in addition, each radio-frequency amplifier stage is tuned to the desired signal, the selectivity of the entire receiver may become very great. In the present congestion of broadcast stations, the necessity for selectivity of a high degree is evident; as we shall see later it is a disadvantage.

128. The wavemeter.—An instrument for measuring the wavelength or frequency of signals is called a **wavemeter** when calibrated in meters or a **frequency meter** when calibrated in kilocycles or cycles. It consists of a coil and a condenser and some means of indicating when this simple circuit is tuned to resonance with a radio wave. The indicator may be a current meter, a lamp which lights up at maximum current through it, or a crystal detector and a d.-c. milliammeter. It may be connected directly into the circuit, or, preferably, coupled loosely to it.

The circuit of a simple and effective wavemeter is shown in Fig. 106. The indicating device is a crystal detector and a meter which indicates the rectified d.-c. current. If it is coupled loosely to the tuned circuit the resistance of this indicator will not broaden the response curve of the wavemeter. The inductance is usually fixed and the capacity varied to obtain resonance, but to cover a wide band of frequencies it is frequently necessary to have several coils which fit into the wavemeter by means of plugs and jacks. If the coils are arranged so that the larger coils have exactly four times the inductance of the next smaller the wavelength range will be doubled, and the frequency range halved.

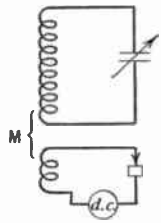


FIG. 106. — A wave meter in which the resistance of the indicator is removed from the tuned circuit and is coupled loosely to it.

A series of coils in which the same winding space is used but in which the number of turns in this space is doubled for each next larger coil will approximate very closely these conditions.

Sometimes the wavemeter is equipped with a buzzer so that it will send out a modulated wave. A receiver can be tuned to a desired frequency by starting the buzzer, tuning the wavemeter to the desired wavelength, or frequency, and adjusting the receiver until the buzzer tones are heard at maximum loudness.

129. Heterodyne wavemeter.—The most useful type of wavemeter is the **heterodyne wavemeter** which uses an oscillating vacuum tube and meter, usually in the grid circuit. The circuit diagram for such a meter is shown in Fig. 107. Tube 1 generates radio-frequency currents, which are modulated when desired by the low- or audio-frequency generator tube 2. Such a meter gives very sharp indications of resonance, and because it is a small modulated source of radio-frequency energy it can be used to tune receivers to any desired frequency. It is a much more accurate instrument than the buzzer wavemeter. The data in Table I are those of an oscillator-wavemeter used in Radio Broadcast Laboratory. The coils are standard General Radio Company inductances (30 to 1000 meters).

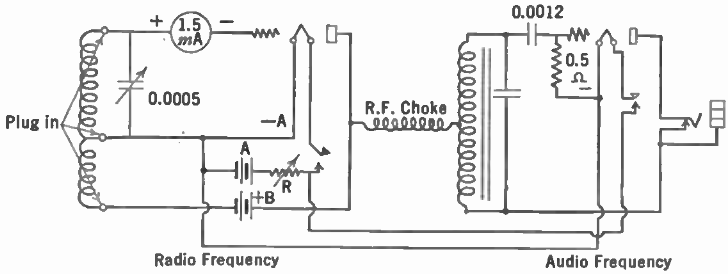


FIG. 107.—Circuit diagram of a heterodyne-wave meter or modulated oscillator.

TABLE I

Coil	λ	f	Kc. per dial degree
15	45–120	2500–6660	31.6
30	80–210	1430–3750	23.3
60	165–400	750–1820	10.7
90	265–620	485–1130	6.5

Coil	Turns	Size Wire	Diameter	Length of Winding	L
277–A	15	21	$2\frac{11}{64}$	$1\frac{5}{8}$	.014 mh.
277–B	30	21	$2\frac{11}{64}$	$1\frac{1}{2}$	.055 mh.
277–C	60	21	$2\frac{11}{64}$	$1\frac{5}{8}$	.217 mh.
277–E	90	27	$2\frac{11}{64}$	$1\frac{7}{8}$	.495 mh.

130. Calibrating a wavemeter.—A wavemeter, or frequency meter, to be most useful must be properly calibrated. This may be done in several ways. If the meter is a heterodyne meter all one needs is a source of known frequency and a receiver. The process is simple. Tune the receiver to a station whose frequency is known. Then turn on the oscillating tube wavemeter, and when a whistle is heard from the receiver, the known station, the receiver, and the wavemeter are all tuned to the same frequency. Then tune the receiver to another frequency and repeat the performance. Then a curve can be plotted showing the calibration of the wave meter.

The following description of how to calibrate a wave meter over a wide range of frequencies by means of but a single accurately known frequency is an interesting experiment. It follows from the fact that an oscillating vacuum tube generates not only the frequency governed by the *LC* product of its circuit but also multiples (harmonics) of this frequency.

Experiment 1–8. To calibrate a wavemeter by harmonics.—The necessary apparatus consists of:

(1) An oscillating wavemeter connected as in Fig. 107.

(2) An oscillating detector tube preferably followed by a stage of audio amplification.

Tune the oscillating detector to the frequency of some known station by listening in the head phones and bringing an antenna wire near the detector inductance. The condenser of the detector should be equipped with a vernier or worm gear so that very accurate settings are possible. Tune as nearly as possible to " zero " beat with the known station. As the tuning dial is adjusted near resonance with the known station, now acting as our frequency standard, a note will be heard in the phones which represents the difference in frequency between the known station and that of the detector tube. When this difference tone (or beat note) disappears, the two oscillations are at the same frequency. Since frequencies lower than about 100 cycles cannot be heard in the phones, it will not be possible to tune closer than this to the desired frequency. By estimating the two points at which the audible beat disappears and finally setting the oscillating receiver detector at the mid-point between these two dial settings, a sufficiently accurate setting will be made.

We have now equipped outselves with a local generator whose frequency is accurately known. For example, suppose it is 610 kc. and that we are set to within 100 cycles of this frequency. We are within 100 parts in 610,000 of being exactly correct or one part in 6100, which is sufficiently accurate. It is much more accurate than we can read the dial on the wavemeter we are to calibrate.

Now move away the antenna coupling and see if the beat note changes. If it does, again adjust for true zero beat. Then start up the oscillating-tube wavemeter and, after giving it a few minutes to warm up, tune its dial slowly until a whistle or beat note is heard in the head phones which are still plugged into the detector-amplifier. This means that the wavemeter is being tuned to the frequency of the oscillating tube.

If we use the broadcast band coil of the wavemeter we ought to get a very loud beat note when the two circuits are in exact resonance and another loud note when the dial is tuned to the half wavelength, in this case 1220 kc. In between these points may be several other weaker beat notes.

TABLE II

Dial Degrees	Difference	Units Difference	*f*—approximate	*f*—exact
10.2*	....	....	1220	1220
34.0	23.8	2	1020	1016
47.0	13.0	1	920	915
60.0	13.0	1	820	813
85.0*	25.0	2	610	610

Now turn the dial slowly and put down on paper each time a beat note is heard. For example, the table of such points may look like Table II, in which the loudest beat notes are marked with an asterisk. Then use another wavemeter coil and repeat, always marking down the loud notes.

Now prepare data like those in the next table, in which the numbers along the top are obtained by multiplying the detector frequency by whole numbers from 1 to 10, and the vertical numbers are obtained by dividing this frequency by whole numbers. Thus our fundamental frequency is 610 kc. Twice this is 1220 kc., one half is 305, etc.

Then make a list from this table of the frequencies that may be looked for from our calibration, namely: 610, 763, 813, 915 kc., etc.

What actually happens as we tune the wavemeter dial and hear beat notes? The oscillating detector and the wavemeter tubes are generating additional or harmonic frequencies as well as the fundamental to which they are set. These additional frequencies are much weaker than the fundamental. When we tune the wavemeter to 1220 kc. it beats with the second harmonic of the detector and gives an audible note. But how are we to recognize the 1220 point? How do we know it is not the third or the fourth harmonic instead of the second?

Consider the data in Table II. We got loud notes at 10.2° and 85°. We guess that these are the second harmonic and fundamental. We subtract the dial settings as in column 2. Then assuming that 13° is a unit, we note that there are two units between the 10.2° and the 34° beat notes. We see then that there are six units between 1220 and 610 kc. We guess again and say that each beat note represents about one-sixth of the difference between 1220 and 610 kc., or about 100 kc. per unit. Looking in our list of expected frequencies we can pick out these frequencies exactly.

TABLE III

	1	2	3	4	5	6
1	610	1220	1830	2440	3050	3660
2	305	610	915	1220	1525	1830
3	202.5	406	610	813	1016	1220
4	152.5	305	457	610	763	
5						
6						

We might guess at these frequencies from the original assumption that the two loud notes were from the 1220 and the 610 kc. frequencies and noting that between them—a difference of 610 kc.—were 85−10.2 dial degrees or about 8 kc. per degree.

When the smaller coils are to be used, care must be taken to see that no harmonics are missed. Fortunately, if the coils have the dimensions given in Table I, the harmonics will fall at almost the same points on the dial. Thus on the largest coil 610 kc. is found at 85°. On the next smaller coil the 1220 kc. frequency will be found within a degree or two of 85°. And so on until the entire set of coils is calibrated.

131. Standard Frequencies.—In this country standard frequency signals are sent out from the Bureau of Standards at stated intervals and can be heard at distances up to 1000 miles from Washington, D. C. In addition there are many long-wave and intermediate-wave stations whose frequencies are kept within very close limits and which are " on the air " 24 hours of the day. The broadcasting stations themselves form good standards of frequency —especially the better known stations—covering the band from 550 to 1500 kc., and above this are many short-wave stations whose signals may be heard the world over.

132. Calibrating by " clicks."—A method of calibration that is often used is the click method. When a tuned circuit is brought near the inductance of the heterodyne wavemeter, a sharp dip of the grid current needle will be noted as the two circuits are resonated to each other. If the same tuned circuit is brought near the inductance of an oscillating detector tube, a sharp click will be heard when the circuits are tuned to the same frequency provided one listens in the plate circuit of this tube or behind a stage of audio amplification. This click is produced by a sharp change in grid current and a corresponding change in plate current.

Experiment 2–8. Calibration by clicks.—This method requires an oscillating detector, a standard meter and the unknown meter to be calibrated.

Couple the standard meter to the inductance of the detector, and turn the dial until a sharp click is heard in the phones indicating that the circuits are tuned alike. If the two inductances are closely coupled two clicks will be heard, one when the tube stops oscillating and one when its starts again. These two points may be several degrees apart. Loosen the coupling, and note that the two clicks approach each other. Keep on loosening it until a degree of coupling is reached when only a single resonance click is noticed. Note the dial setting of the standard meter. Now remove it from the tuned circuit and bring near the latter the wavemeter to be calibrated. Turn its condenser dial until a click is heard as before. Now the meter has the same frequency, or wavelength, as the standard. Other points for a calibration curve may be noted in the same manner.

This method really constitutes setting a generator or miniature transmitter (the oscillating detector) to a given frequency by means of the standard meter and then tuning the uncalibrated meter to resonance with this generator.

133. The properties of coils and condensers.—We may investigate the properties of coils and condensers by performing the various parts of the following experiment.

Experiment 3–8. Wind up on a form about 3 inches in diameter, a coil of about 60 turns of rather large wire, preferably with silk or enameled insulation so the distributed capacity of the inductance will be rather large. Connect it across a condenser whose maximum capacity is about 500 mmfd. Starting

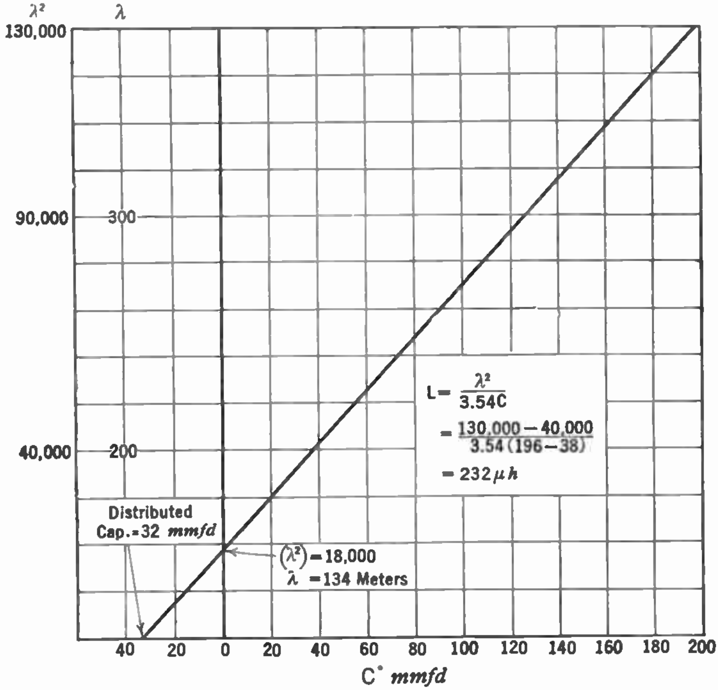


FIG. 108.—A method of determining the distributed capacity of a coil.

at the maximum capacity of the condenser, measure the resonant frequency of the coil-condenser combination by "clicking" it into an oscillating receiver, or by coupling it to an oscillator. Then decrease the capacity and repeat until several readings are taken, say at 500, 400, 300, etc., mmfd. Plot the result against C as shown in Fig. 108; that is (wavelength)^2 against capacity.

A straight line results because the formula

$$(\text{Wavelength})^2 = 3.54\, L \times C,$$

where L is in μ h and C in mmfd., is the equation of a straight line and states that the wavelength squared is proportional to the capacity in the circuit. The slope of the line divided by 3.54 is the inductance of the coil, that is,

$$L = \frac{1}{3.54} \times \frac{\lambda^2}{C}.$$

It will be noticed that the straight line crosses the wavelength squared axis at some distance above the zero point. This gives us the natural wavelength squared of the coil itself and therefore the resonant wavelength to which the coil with no additional capacity will tune. The point where the line crosses the capacity axis gives us the distributed capacity of the coil. This value multiplied by the inductance as obtained above gives the LC product which when fitted into the proper formula gives the natural wavelength of the coil.

Thus, in one experiment we can determine not only the frequency or wavelength to which a coil-condenser combination will tune, but we can determine the coil's inductance, its distributed capacity, and its natural wavelength.

As a check on these data: (a) calculate the inductance from the formulas given in Fig. 51. (b) If a heterodyne wavemeter is available and calibrated to short wavelengths, detach the condenser from the coil and click the latter into it, and thereby determine the natural wavelength of the coil.

134. Measurement of coil resistance.—The effect of resistance upon the sharpness of resonance and the selectivity of the circuit has been mentioned (Section 112). The **resonance curve** gives us one method of measuring the resistance in a given circuit, provided we know the inductance of the coil—which can be calculated from the formula in Fig. 51.

Experiment 4–8. To determine the resistance of a coil.—Couple a series circuit composed of a coil, condenser, and indicating meter to a generator of about 5-watts output. Adjust the frequency of the generator through resonance with the series circuit. If the generator has a constant output over this frequency range the accuracy with which the coil resistance is determined will be greater. Pick out the two frequencies above and below resonance where the current in the circuit is .707 of its value at resonance and calculate the width of frequency band at this point and the resistance of the circuit, from the equation

$$R = \frac{L\omega\,(f_2 - f_1)}{f_r}.$$

Subtract from this value the resistance of the current meter. For example a model 425 Weston thermo-galvanometer will read currents of 115 milliamperes and has a radio-frequency resistance of 4.5 ohms. The value of resistance remaining is the resistance of coil, leads, and condenser. Most of this resistance resides in the coil.

Experiment 5-8. To determine resistance of a circuit.—Another method of determining the resistance of a coil is as follows. It necessitates the use of a decade resistance box or series of accurately known resistances of negligible inductance and capacity and a variable condenser.

Small lengths of high-resistance wire (manganin) are to be preferred for frequencies higher than 1000 kc. Their d.-c. and high-frequency resistance is practically the same.

Connect the apparatus in series and couple to an oscillator.

With the resistance box short-circuited ($R = O$), tune the circuit to resonance. Then add enough resistance to the circuit to halve the current, retuning to resonance, if necessary. Then since we have halved the current, Ohm's law tells us that we have doubled the resistance. In other words the added resistance is equal to the resistance already existing in the circuit. Again subtract the resistance of the current-indicating meter. What remains is the resistance of coils, condensers and leads.

Repeat at several different frequencies and calculate the "sharpness of resonance," $L\omega/R$, and plot against frequency and wavelength.

If only one or two resistance units are available, say 5 or 10 ohms and not a continuously variable standard of resistance like a decade box, the resistance of the circuit above may be determined by noting the current at resonance, and the current when some resistance has been added, retuning to resonance after adding the resistance if necessary. Then the current, according to Ohm's law, is

$$I_1 = \frac{E}{R_1}$$

$$I_2 = \frac{E}{R_1 + R_2},$$

where I_1 = current at resonance and no added resistance;

I_2 = current at resonance and R_2 added;

R_1 = resistance of circuit;

R_2 = added resistance;

whence

$$R_1 = \frac{R_2 I_2}{I_1 - I_2}.$$

If a current-indicating meter is used whose deflections are proportional to the current squared, an example is a thermogalvanometer or a hot-wire meter, it is only necessary in this experiment to add sufficient resistance to quarter the deflection of the instrument. This is equivalent to halving the current, and the added resistance is equal to the resistance already in the circuit.

The lower the resistance of the current-indicating device, the greater will be the accuracy with which such measurements may be carried out. For example, if the indicator has a resistance of 4.5 ohms and the circuit a resistance of 5 ohms, great accuracy cannot be attained, but if the circuit resistance is double or treble that of the indicator, much greater accuracy results. In any case the meter resistance must be subtracted from the measured resistance to get the resistance due the circuit alone.

135. Condenser capacity.—We will now investigate by means of an experiment the capacity of a condenser.

Experiment 6–8. To determine the capacity of a condenser.—Connect a variable condenser whose calibration is known across a coil and click into an oscillating receiver or into a heterodyne wavemeter; attach the unknown condenser across the variable condenser and retune the latter to resonance with the wavemeter. The difference in readings of the calibrated condenser is the capacity of the unknown condenser. For example, suppose resonance is obtained by the variable condenser alone when set at 400 mmfd. Connecting the second condenser across the variable forces us to reduce the capacity of the latter to 340 mmfd. The difference 400 − 340 = 60 mmfd. is the capacity of the unknown. Such a method enables the experimenter to disregard the capacity of the coil itself or of the leads since these are connected across the variable at all times and do not change when the unknown is attached to the circuit.

136. Antenna wavelength.—We will proceed to determine the wavelength of an antenna by means of the following experiment.

Experiment 7–8. To measure the natural wavelength of an antenna.—Connect in series with the antenna an inductance which can be adjusted in even steps, say a coil of 20 turns with taps at each turn. Measure the frequency to which the antenna tunes with the entire coil in the circuit by coupling the coil to a heterodyne wavemeter. Then reduce the inductance by one turn, and repeat. Repeat until accurate readings are no longer possible. Plot wavelength, or frequency, against added turns of wire. Where the line crosses the wavelength or frequency axis is the natural wavelength or frequency of the antenna.

137. Antenna capacity.—The capacity of an antenna may also be determined by experiment.

Experiment 8–8. To measure the capacity of an antenna.—Measure the wavelength of an antenna attached to an inductance, as in Fig. 109. Then replace the antenna-ground connections by a variable condenser (Fig. 109*b*) and tune the condenser until resonance with the wavemeter is indicated. The capacity of the condenser at this point is the capacity of the antenna.

138. Antenna inductance.—Experiment is resorted to to determine the inductance of an antenna.

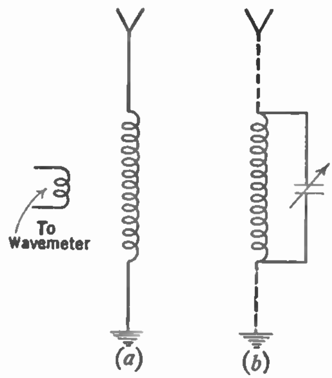


FIG. 109.—To measure capacity of an antenna.

Experiment 9–8. To determine the inductance of an antenna.—Connect a known inductance, L_1, in series with the antenna and measure the wavelength λ_1. Repeat, using a different inductance L_2 and get λ_2. Then the two wavelengths are related as below.

$$\lambda_1 = 1.884\sqrt{(L_1 + L_a)C_a}$$
$$\lambda_2 = 1.884\sqrt{(L_2 + L_a)C_a}$$

where L_a = antenna inductance in microhenries;
C_a = antenna capacity in micro-microfarads.

Eliminating C_a between these two equations we get

$$L_a = \frac{L_1\lambda_2^2 - L_2\lambda_1^2}{\lambda_1^2 - \lambda_2^2}.$$

Problem 1–8. A wavemeter is being calibrated from a standard. At resonance the capacity of the standard is 400 mmfd., the capacity of the the other meter is 500 mfd. What is the ratio of their inductances? If the inductance of the standard is 300 microhenrys, what is the inductance of the other wavemeter? At what frequency are they now set? What is the wavelength?

Problem 2–8. A coil and condenser combination has a resistance of 8 ohms at 300 meters. What is the width of the frequency band at the points below and above resonance where the current is 0.707 of its resonance value? The inductance is 250 microhenrys.

Problem 3–8. In an experiment to determine the resistance of a coil by the change of total resistance method (Experiment 5), the current without added resistance is 100 milliamperes and with 12 ohms added it is 60 milliamperes. The resistance of the meter is 5 ohms. What is the resistance of the coil and condenser in series?

Problem 4–8. A certain coil-condenser (LC_1) tunes to a frequency, f_1. The condenser is changed by adding another to it so that the value is C_2. The circuit now tunes to a frequency, f_2. Prove that $\frac{f_2}{f_1} = \frac{\sqrt{C_1}}{\sqrt{C_2}}$.

Problem 5–8. Using the formula in Problem 4, what must be done to the capacity to make a circuit tune to twice the frequency, half the frequency, double the wavelength, one-half the wavelength?

Problem 6–8. A coil-condenser combination tunes to 450 kc. when the condenser is 600 mmfd. When an unknown condenser is placed in series with the 600-mmfd. capacity the circuit tunes to 600 kc. What is the unknown capacity?

Problem 7–8. An antenna tunes to 300 meters when 100 microhenrys are in series with it, and 400 meters when 300 microhenrys are in series. What is the inductance of the antenna? Remembering that the two inductances, L_1 or L_2, and the inductance of the antenna L_a are in series, and can be added to get the total inductance, what is the capacity of the antenna? What is its natural wavelength?

139. Typical receiving circuits.—The first essential of all receivers is an antenna to collect energy from the distant station. This can be a single wire stretched out in the open. For broadcast-frequency receivers under average conditions, it should be about 60 feet long. In order that a receiver may be transferred to other antennas without the difficulties due to changes in tuning, some engineers have eliminated the antenna from the tuning of the set, and use it only as a collector. It is usually loosely coupled to the receiver, so loosely, in fact, that very little energy is transferred at the lower frequencies where the coupling is weakest. It is here that tuning the antenna to series resonance with the incoming signals helps considerably toward boosting their strength, and at times the practice of series tuning the antenna has been employed. Because of the distributed capacity of the coil and the minimum capacity of the condenser as well as the capacity of apparatus attached to the coil-condenser combination the lowest wavelength that can be attained without changing the circuit is limited. The ratio of longest to shortest wavelength received on broadcast tuners is about 3 to 1, that is, from 200 to 600 meters. Because the wavelength varies as the square root of the capacity, the capacity range of the condenser must be nine to one. If the maximum capacity of the condenser is 500 mmfd., a maximum of

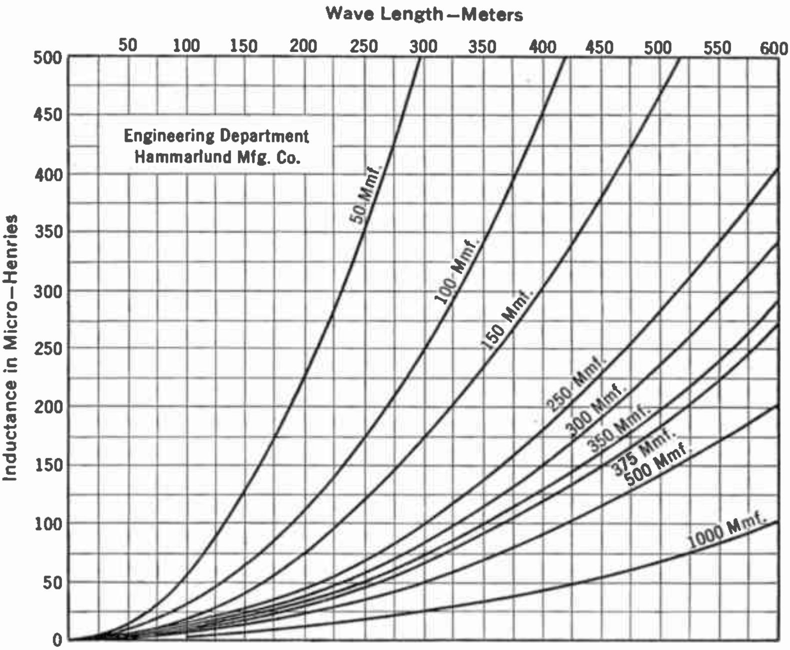


Fig. 110.—Curves showing the amount of capacity and inductance to tune to a given wave length.

50 mmfd. can be across the inductance when the condenser is turned to zero degrees and still cover the required frequency range. This capacity is made up of the coil capacity, minimum capacity of the tuning condenser, leads, etc.

The resistance of the coil has an important bearing upon selectivity and to some extent upon the sensitivity of the receiver. As we shall see later it has an important bearing upon the fidelity, or quality, of signals as they emerge from the loud speaker. The resistance of modern variable condensers may be neglected. The resistance introduced into coils and accessory circuits by large nearby metallic masses may be considerable, and therefore coils, if shielded, must be kept at a respectable distance from the metallic shielding material.

Modern receivers usually possess from two to four stages of amplification at radio frequencies, and from one to three stages of audio-frequency amplification. In general the more radio stages

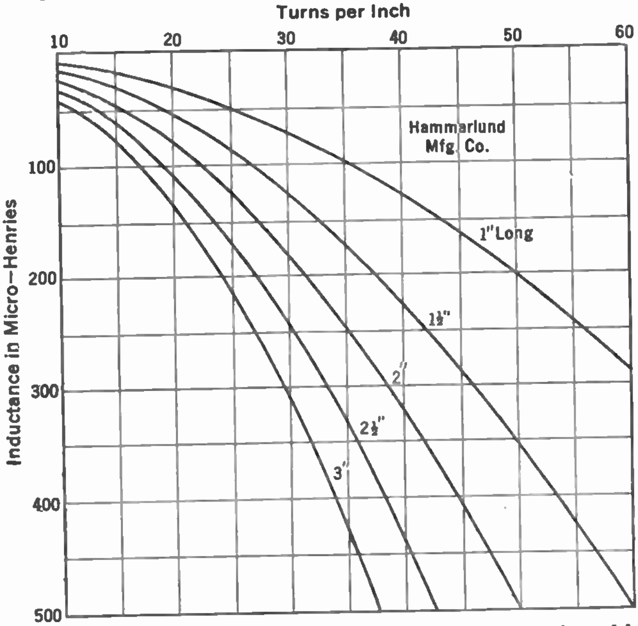


FIG. 111.—Curves showing the inductance of a coil as a function of length of winding and turns per inch.

the more selective and sensitive the set will be, but the number of tubes is no criterion as to the set's ability to get weak distant distant stations through strong local interference. A well engineered receiver of four tubes may be much better than a poorly designed receiver of eight tubes. The difference lies not in the number of tubes but in the design and subsequent engineering.

The manner in which L, C, λ, and coil dimensions are related is plotted in Fig. 110 and Fig. 111.

read to 188.

CHAPTER IX

THE VACUUM TUBE

THE most important single device known to radio science is the **vacuum tube.** Although it is true that some receivers exist which use no tubes at all, and that those which are within a very short distance of broadcasting stations and which use only head phones can get along with a coil, a condenser, and a crystal detector, far the greater number of receivers in this country use tubes, some of them one, some two, many as high as twelve or more.

140. The construction of the vacuum tube.—As we know the tube today it consists of a glass wall within which are three metallic parts known as the elements. In the center is the **filament** which may be made of tungsten, carbon, tungsten covered with thorium, platinum or nickel coated with oxides of barium, strontium, caesium, and other chemical elements. Next to the filament is the **grid**, an open mesh of molybdenum (frequently) wire screen; finally is the **plate** which is a sheet or screen of metal, often of nickel. Some tubes have only two elements, the filament and the plate; many have an additional grid; the mechanical construction differs according to type of tube, its use, and its manufacturer.

After the various elements are placed within the tube, the glass wall is attached to a pump and the gas is removed. During the pumping process the glass wall is heated in an electric oven to drive out the gas from it, and later the elements are heated by means of an "induction furnace" so that various gases bound up in these metals may be pumped out. The modern tube is a high vacuum tube; early types were poorly pumped and were really gaseous tubes, tubes which would be rejected by modern testing methods. When the pumping or "exhaustion" process is complete the glass wall and its contents are sealed. Then the tube goes through several electrical tests and inspections before it can be labeled, packed, shipped and again unpacked and sold for use.

141. The purpose of the filament.—In Chapter I of this book we discussed the electron, that elementary constituent of matter which carries electricity. Little has been said about the electron in subsequent chapters; now it enters again and assumes an important rôle. The filament is the heart of the vacuum tube; the electrons which rush about in this filament are the life blood. When the filament is dead—due to age or crossed wires—the electrons no longer move in the proper manner; the tube is dead and might as well be broken up. If a filament of tungsten is heated so that an individual electron gets up a speed of 1×10^8 centimeters per second (620 miles per second) it can break through the surface tension of the filament. Since it is negatively charged it will be attracted toward any positive body nearby.

142. The purpose of the plate.—When the electron is released from the filament it goes shooting out into the void in which the elements are situated. When it leaves the filament, it takes with it a negative charge, and thereby leaves the filament positively charged. If there is no body at a positive potential within the bulb other than the filament, the electron will eventually find its way back to the source whence it came. If, however, a "plate" is within the tube and is more positive than the filament, the electron will be attracted to it. Even when the plate is at the proper positive potential to attract many electrons, some go back to the filament, and others congregate somewhere between the filament and the plate and constitute what is called the "space charge."

Every electron which hits the plate constitutes a minute electric current and when enough of them arrive per second a measurable current is attained. It is this current carried by the electrons from the filament which constitutes the tube's plate current which is used in so many ways. The symbol for plate current is I_p; the plate current is usually measured and expressed in milliamperes.

The source of the electrons is usually called the filament although some modern tubes get their supply of electrons in another manner, as indicated in Section 166. This filament is heated by a battery, called an **A battery,** or by a small step-down transformer from the a.-c. lighting circuit. A battery inserted between part of the filament system and the plate maintains the plate positive with respect to the filament. It is called the **B battery.**

When the filament is heated to a proper temperature a copious stream of electrons is emitted. Some of the electrons are attracted to the positive part of the filament, that is, to the side of the filament, that is attached to the positive end of the A battery. If the plate is insulated from the filament, a few electrons will get through the fog called the space charge but if it is at a higher potential than the filament it attracts many more electrons. It is

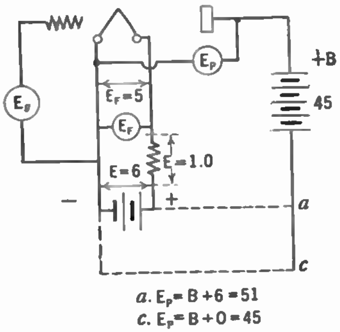


Fig. 112.—If the B battery is connected as at (*a*) the voltage on the plate is 51 volts; if as at (*c*) the voltage is 45.

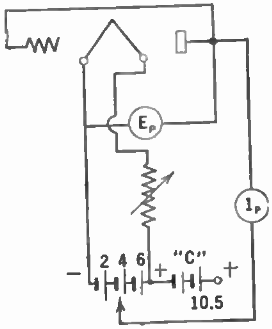


Fig. 113.—Circuit for testing effect of plate voltage on emission.

usually so maintained by means of the B battery and in some cases may be as high at 10,000 volts above the potential of the filament. This B battery may be attached to the filament in several ways. Its negative end may be connected to the negative end of the A battery or to the positive end of the A battery. It is standard practice in the telephone plant to connect A plus and B minus together; in other places it is common practice to connect the two negative leads together. The most negative part of the filament in the case of d.-c. tubes, or the center of the filament in the case of tubes run from a.c., is considered as the point to which all other voltages are referred. (See Fig. 112.)

Experiment 1-9. Effect of plate voltage on a two-element tube.—Connect the grid and plate of an ordinary receiving tube together and connect into a circuit as shown in Fig. 113. Use a plate-current meter reading about 5 milliamperes. Light the filament and read the plate current as the plate is connected to the negative end of the battery and then to plus 2, 4, and 6 volts by connecting it to the first, second, or third storage cell in the battery. Connect the negative terminal of a 4.5-volt C battery to the positive end of the A battery and the positive terminal of the C battery to the plate. Read the plate current. The plate is now plus 10.5 volts above the potential of the negative part of the filament. Explain why.

143. Effect of filament voltage.—The experiment above shows that the effect of increasing the positive potential of the plate is increase the flow of electrons. The filament temperature, too, has an important effect upon the flow of electrons. The hotter the filament the more electrons per second will be released into the space surrounding the heated element. If, however, the voltage on the plate is low, there will soon be reached a definite plate current which cannot be exceeded no matter how hot the filament becomes. In other words the plate is taking all the electrons it can get through the space charge. It is true that more electrons leave the filament at higher temperatures but they simply add to the space charge or return to the filament. If the plate battery voltage is increased, a greater plate current will flow, but again a point will be reached where passing more current through the filament ceases to increase the plate current. Typical saturation curves for a 201 A type of tube are shown in Fig. 114. Whenever the space charge (negative) is more effective in repelling electrons than the plate (positive) is in attracting them a flattening plate current takes place.

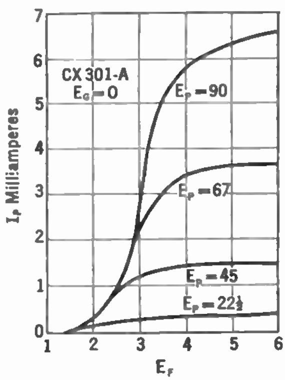


Fig. 114.—Saturation curves.

Experiment 2-9. Effect of filament voltage: Three-element tube.—A study of many of the tube's characteristics may be made with a set-up of apparatus like that in Fig. 115 which consists simply of a board upon which are connected several Fahnestock clips to which may be attached meters and batteries of the proper potential. A good voltmeter is a two-range Weston Model 506 reading on the low scale up to 7.5 volts and on the upper to 150 volts. Jewell pattern 77 is a similar meter. These will read the ordinary ranges of filament and plate voltages. A plate current meter may be any milliammeter reading from 5 milliamperes upward.

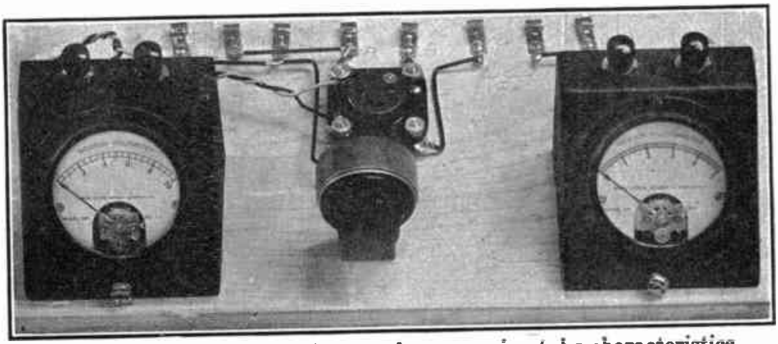


Fig. 115.—An experimental set-up for measuring tube characteristics.

Connect up a tube as shown in Fig. 116 and after reading the plate voltage, place the meter across the filament. Use at the start about 22.5 volts of B battery. Turn on the rheostat slowly and read the filament voltage and plate current. If either meter should read backwards, reverse it. Plot as in Fig. 114 the relation between E_f (filament volts) and I_p (plate current). Increase the plate voltage and repeat.

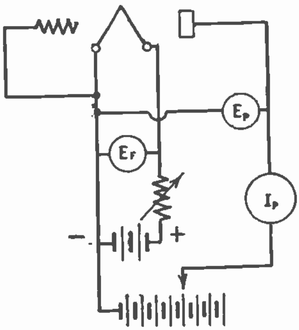


Fig. 116.—Circuit for apparatus of Fig. 115.

144. Saturation current.—With a given filament voltage (which produces a certain filament temperature) more and more electrons will be drawn to the plate as the voltage of the latter is increased—up to a certain point. But beyond this point additional plate voltage has little effect on plate current and the plate current curve flattens out. All of the electrons emitted by the filament are being taken by the plate and increasing the plate voltage has no effect upon the number of electrons emitted. Increasing the filament temperature produces an additional supply of electrons, and the plate current will again increase.

Experiment 3–9. Effect of plate voltage: Three-element tube.—Connect up the apparatus used in Experiment 2 as shown in Fig. 116. Set the filament voltage at some fixed value and take data showing the effect upon plate current of varying the plate voltage. Increase the filament voltage and repeat. Plot the data in a manner similar to that in Fig. 114. Remembering that 6.28×10^{18} electrons per second flowing past a certain point in a circuit constitutes an electric current of an ampere, calculate the number of electrons that arrive at the plate per second for several values of filament and plate voltage.

The experiments and curves above show

1. The relation between plate and filament voltage and plate current.

2. The saturation effect at low filament and plate voltages. Saturation due to insufficient plate voltage is known as filament saturation; that due to insufficient electron supply is called plate saturation.

3. The fact that little is to be gained by increasing the filament voltage above the rated value.

4. The curve connecting plate current (I_p) and filament voltage (E_f) is not a straight line.

This shows that Ohm's law is not being followed; the law in fact is much more complicated. The plate current is zero at zero filament voltage, and as the latter is increased the plate current begins to rise too, but not in a straight line. Soon, however, the negative space charge built up by the electrons which do not get to the plate prevents any more electrons getting to the plate. The plate current then is limited, and may be increased only by increasing the plate voltage so that it is again more positive than the space charge is negative. Various means are used to overcome this space charge which shall be discussed later.

145. The purpose of the grid.—The third element, for which DeForest is famous, is the grid, the mesh of wires between the filament and plate. It has several important uses. It may be used to neutralize the space charge so that greater plate current may flow with a given filament temperature and given plate voltage.

Suppose the grid is made positive with respect to the source of the electrons. Since it is physically nearer the filament than is the plate, a small positive potential will have the same effect as a large positive potential on the plate. A positive potential near the filament accelerates the escape of electrons, and prevents the building up of a high negative space charge and then the plate has a greater ability to attract the carriers of electric current.

Suppose, however, we make the grid negative. Owing to its relatively close position with respect to the source of electrons, a small negative voltage on it will counteract a large positive voltage on the plate. So, with a small negative voltage we can prevent any electrons from getting to the plate, or by varying this grid voltage we can regulate in any desired way the number of electrons that reach the plate, and thereby control the plate current. Since there is no time lag in the flow of electrons, the grid voltages take instantaneous effect upon the plate current. The grid, then, is a control electrode. The relation between the effects upon plate current of the grid voltage compared to the plate voltage constitutes an important tube " constant," the amplification factor.

146. Characteristic curves.—In the average receiving tube there are three electrodes. The filament has already been mentioned, and the manner in which its temperature affects the plate current has been tested. The plate and the effect of its voltage on plate current have been qualitatively mentioned; so has the effect of grid voltage. Under ordinary conditions the filament is operated " saturated," that is, at such voltage that there is little use in raising it further. Its voltage is then fixed; it is not varied.

If the filament voltage is considered as fixed, we still have the plate current depending upon two variable quantities, the grid and the plate voltage (E_g and E_p). The manner in which these variables affect the plate current controls the characteristics of the tube. When plotted in graphs, they are called **characteristic curves.**

Experiment 4–9. Effect of grid bias upon plate current.—Set up the apparatus as shown in Fig. 117, using in succession several of the common types of tubes. Set the filament at the proper voltage. Fix a small voltage, say 22.5 volts, on the plate of the tube and take down data showing how the plate current changes as the grid bias is varied from a point where the plate current is zero to a grid voltage of about positive 10 volts. The D. P. D. T. switch in the grid circuit makes possible changing the polarity of the grid without changing the meter (E_g) connection. Then raise the plate voltage and repeat. Plot these data like those in Fig. 118.

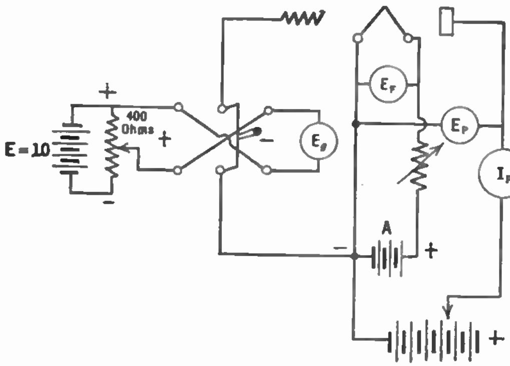


Fig. 117.—Complete apparatus for measuring characteristics. The D. P. D. T. switch reverses the grid voltage.

147. Grid voltage—plate current curves. — Several interesting and important facts may be discovered by looking at such curves which we shall call the E_g—I_p curves. At large negative grid voltages there is little or no current in the plate circuit. As this negative voltage is decreased, some electrons get past the grid and through the space charge and to the plate. The current begins to flow, increases at a rather slow rate, then more rapidly, then in a steep and straight line, and finally, if the experiment is

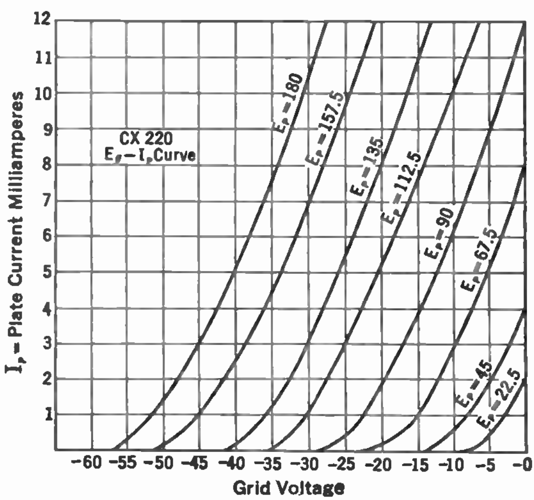


Fig. 118.—A family of E_g-I_p curves.

carried far enough, the curve flattens out. Increasing the plate potential and again varying the grid potential produces a new curve which is essentially parallel to the first, but moved to the left. Increasing the plate voltage again a like amount produces a new curve displaced an equal distance to the left of the second line. Such a graphic collection of data is known as a "family" of curves and tells all we need to know of the effect of grid voltage upon plate current. Grid voltages may be secured from a battery known

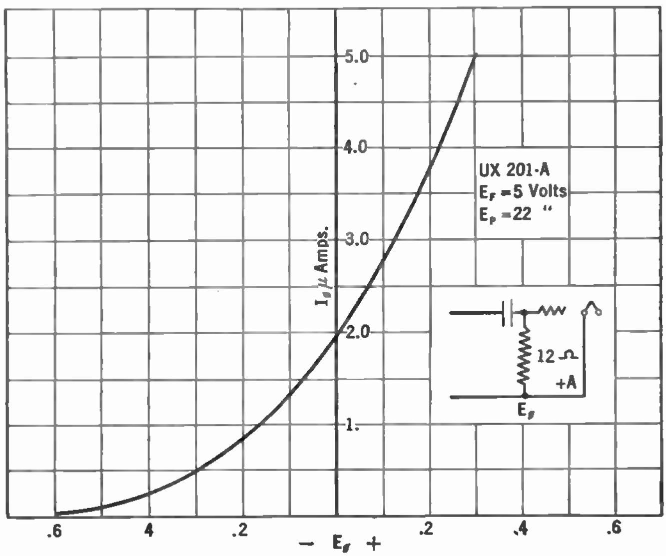


Fig. 119.—Grid current curve of a commonly used tube.

as a C battery and the voltage itself is frequently called a "C" or grid "bias."

If we place a meter in the grid circuit at the same time the plate current is measured, we shall see that a very small grid current is taken at positive grid potentials. This current in ordinary practice is very small, seldom over one-tenth of the plate current, and in all amplifiers in which the minimum distortion is desired the current in the grid circuit is kept as low as possible by making the grid highly negative. The grid current curve for a typical case is shown in Fig. 119.

148. The effect of plate voltage upon plate current.—To determine this effect we will resort to experiment.

Experiment 5–9. Set up the apparatus as in Experiment 4. Set the grid voltage at some value, say minus 5 for an ordinary receiving tube, and note down the plate current as the plate voltage is changed from 0 to perhaps 100 volts. Then change the grid voltage to minus 10 and repeat; then at minus 15 and 20; 0, and plus 5 and 10, etc.

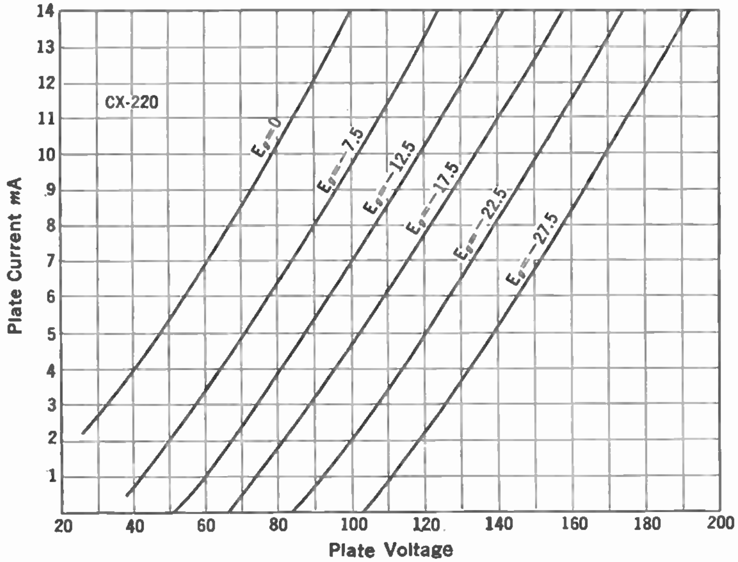


Fig. 120.—Plate current—plate voltage curves.

These data may be taken from the $E_g - I_p$ curves plotted in Experiment 4 by picking off the curves the proper values of current, and plate and grid voltages.

149. Plate voltage—plate current curves.—Here again (Fig. 120) the curves which we shall call the I_p curves are essentially parallel over the straight parts. If the grid voltages chosen are in equal steps, the plate current curves will be equal distances from each other.

From characteristic curves of this type, we may calculate all of the tube's constants, and foretell nearly all of its properties when connected into a circuit with other apparatus whose electrical constants we know.

150. Amplification factor.—For example we know that the grid potential is relatively more important in controlling plate current than is the plate voltage. Why? Because it is nearer the source of

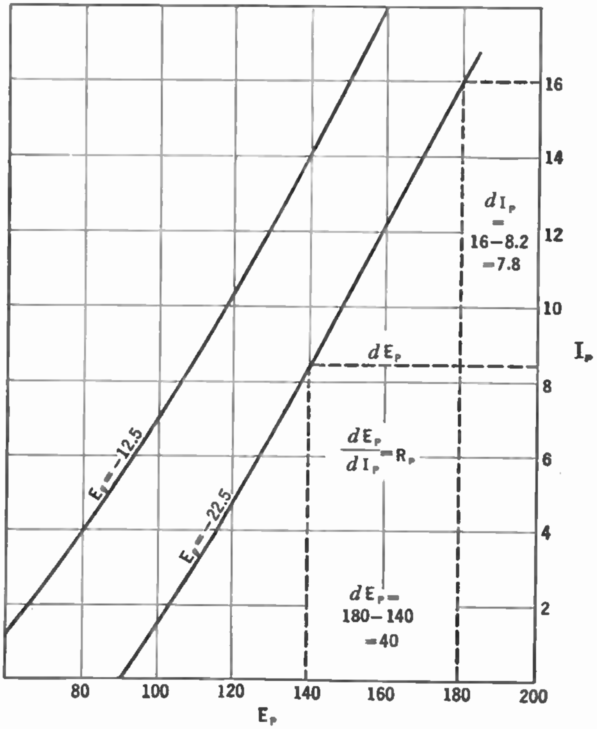


Fig. 121.—Detailed E_p-I_p curve showing how to calculate R_p.

electrons. How much? We can tell from the E_p—I_p curves in Fig. 121. Looking at the line marked $E_g = -22.5$ only, we see that at a plate voltage of 180 the plate current is 16 milliamperes but that if E_p is decreased to 140 volts the plate current decreases to 8.2 milliamperes—a change of 7.8 milliamperes for 40 volts or a net change of 0.195 milliampere per volt. This is the slope of this particular line and, as we shall see later, it gives us another important tube constant without further calculation.

Now looking at the two curves marked $E_g = -12.5$ and $E_g = -22.5$ at the points where they cross the 140-volt E_p line, we see that at this value of plate voltage the plate current is respectively 14.0 and 8.2 milliamperes at these two values of grid voltage. This means that changing the grid voltage by 10 volts causes a change of 5.8 milliamperes in the plate current, a net change of 0.58 milliampere per volt. Dividing the change per volt caused by E_g variations, by the change per volt produced by E_p variations gives us the relative ability of the grid and plate potentials to influence the plate current. Thus,

$$\frac{\text{Ability of grid voltage to control plate current}}{\text{Ability of plate voltage to control plate current}}$$

$$= \frac{0.58 \text{ ma./volt}}{0.195 \text{ ma./volt}} = 3.0.$$

This ratio is defined as the amplification factor of the tube. It is the ratio between the plate voltage change required to produce a certain plate current change and the grid voltage change required to produce the same change in plate current. The Greek letter mu, μ, is the symbol used in the literature for the amplification factor of a tube. Thus

$$\mu = \frac{\text{plate voltage change to produce a given plate current change}}{\text{grid voltage change to produce the same plate current change}}.$$

The amplification factor for a given tube does not vary much under the conditions under which the tube is ordinarily used. It is controlled largely by its mechanical construction, and the nearness of the grid to the filament. A grid composed of many wires close to the filament produces a high amplification factor; a tube with a wide mesh and not so close to the filament produces a tube with a low amplification factor.

The student should note that the amplification factor is *not* the ratio between plate and grid voltages, but is the ratio between *changes* in these voltages. It may be expressed in more mathematical language as

$$\mu = \frac{dE_p}{dE_g} \text{ to produce a given } dI_p,$$

where the prefix " d " signifies " a change in " (a differential).

The amplification factor may be obtained from the E_g–I_p curves in Fig. 121 in a manner similar to that outlined above. It is also equal to the change in I_p produced by, say, 10 volts change in E_g divided by the change in I_p produced by 10 volts change in E_p. Thus in Fig. 120 changing E_g from $-$ 22.5 to $-$ 12.5 (with $E_p = 140$) produces a variation of 5.8 milliamperes while along the $E_g = -$ 22.5 line a change of E_p from 140 to 150 volts produces a variation of 1.95 ma.

$$\text{Then } \mu = \frac{5.8}{1.95} = 3.0 \text{ as before.}$$

151. The meaning of the amplification factor.—If the amplification factor of a tube is 3, for example, adding 30 volts to the plate will increase the plate current a certain amount. Adding only 10 volts (positive) to the grid will produce the same plate current change. That is, adding 10 volts negative to the grid will bring the plate current back to its value before the plate voltage had been increased. In other words any voltage placed on the grid of such a tube has the same effect as a voltage in the plate circuit multiplied—or amplified—by the μ of the tube. A voltage E_g on the grid becomes equal to μE_g when it gets to the plate circuit.

152. Equivalent tube circuit.—Since a change in plate voltage may be replaced by a smaller change in grid voltage multiplied by the μ of the tube, we may replace the entire tube by a fictitious generator whose voltage is μE_g and whose internal resistance is equal to the resistance of the tube. In fact in all problems the tube is so considered, and is indicated symbolically as in Fig. 122.

Problem 1–9. With a 20-volt bias the plate current of a tube under a given value of E_p is 55 ma., and when the bias is increased to 30 volts the plate current is reduced to 28 ma. If, however, at this value of grid bias (−30) the plate voltage is increased from 180 to 210 volts the plate current comes back to its original value, 55 ma. What is the amplification factor of the tube?

Problem 2–9. The amplification of a tube is 8 and when the grid is − 3 volts the plate current is 3 ma. If the bias is reduced to zero the current increases to 8 ma. Both of these current values were read when the plate voltage was 90 volts. How much would the plate voltage have to be reduced (at zero grid bias) to bring back the current to its 3 ma. value?

Problem 3–9. Changing the plate voltage of a power tube from 100 to 300 volts changes the plate current from 10 to 55 ma. If the bias is zero at the latter figure what must be done to it to reduce the current to its former value if the amplification factor is 7.8?

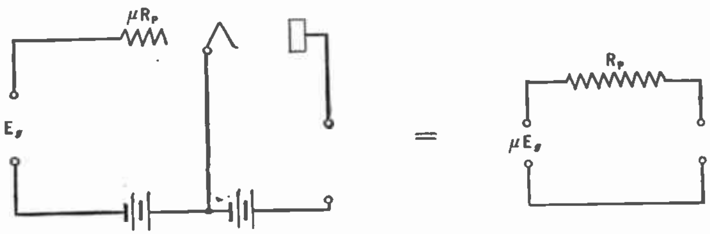


Fig. 122.—The tube and its equivalent circuit; a voltage μE_g in series with R_p and the load.

153. D.-c. resistance of a tube.—Since a certain plate current flows under the pressure of a certain plate voltage, the ratio

$$R = \frac{E_p}{I_p}$$

in which E_p = the d.-c. voltage on the plate;
I_p = the d.-c. current in the plate circuit,

gives the d.-c. resistance of the space between the filament and the plate. The power used up by the electronic current may be found by multiplying the plate voltage by the plate current, or

$$P = I_pE_p \quad \text{or} \quad \frac{E_p^2}{R} \quad \text{or} \quad I_p^2R.$$

This power is the rate at which the kinetic energy possessed by the moving electrons is given up to the plate. When the electron leaves the filament it is attracted toward the plate, increasing in speed as it gets closer and closer to the positive potential which is the attracting force. When the electron hits the plate its kinetic energy due to its motion is given up. In a transmitting tube the number of electrons that arrive per second may be so high that the plate becomes red- or white-hot.

154. Internal resistance of the tube.—This d.-c. resistance is not what is popularly known as the "**impedance**" of the tube, or more properly called its "**plate resistance**" or "**differential or internal resistance.**" The latter is the ratio between a *change* in plate voltage and the *change* in plate current produced by this change in plate voltage. It is the resistance offered to the flow of a.-c. currents in the plate circuit and is not the same resistance as is offered to the flow of d.-c. current from the battery. Then

$$R_p = \frac{\text{change in plate voltage}}{\text{change in plate current}} \quad \text{or} \quad \frac{dE_p}{dI_p}.$$

For example changing the plate voltage from 180 to 140 volts (Fig. 121) produced a plate current change of 7.8 milliamperes (0.0078 ampere)

$$R_p = \frac{dE_p}{dI_p} = \frac{180 - 140}{.016 - .0082} = \frac{40}{.0078} = 5200 \text{ ohms (approx.)}.$$

Problem 4–9. Make a table showing the d.-c. resistance of various tubes in general use at the conditions they ordinarily work, that is, a 201-A tube at $E_p = 90$ volts and $E_g = -4.5$, a 171 with $E_p = 180$ and $E_g = -40.5$. Use values of plate current in the tube chart. Compare the d.-c. resistance with the a.-c. resistance.

Problem 5–9. The plate current of a tube is 4.5 ma. when $E_p = 90$ volts, and is equal to 0.9 ma. when $E_p = 40$ volts. What is the plate resistance?

Problem 6–9. The plate resistance of a tube is 12,000 ohms. At $E_p =$ 140, $I_p = 14.5$ ma. What is I_p when $E_p = 100$ volts?

Problem 7–9. Calculate the d.-c. resistance of the tube under the two conditions of E_p and I_p in Problem 6, and the power used in heating the plate.

The internal resistance changes with plate and grid voltages and so the conditions of both must be considered when the resistance is mentioned. Thus the UX 171 has an internal resistance of 2000 ohms when the plate voltage is 180 volts, and the grid voltage is 40.5 volts negative. Its internal resistance differs if either E_p or E_g is varied.

The student should note that R_p is not the ratio between a plate voltage and a plate current but is a ratio between *changes* in both plate current and plate voltage. Thus a 201–A tube at a plate voltage of 90 has a plate current of 2.5 ma. The ratio $\frac{90}{.0025} = 36{,}000$ ohms is the d.-c. resistance; R_p is equal to about 13,000 ohms under these conditions.

155. Mutual conductance of a tube.—There is one more important tube constant, the **mutual conductance.** This is the factor which tells us how much plate current change is caused by a given grid voltage change. Thus

$$G_m = \frac{\text{change in plate current}}{\text{change in grid voltage}} = \frac{dI_p}{dE_g}$$

Thus if a change of one grid volt produces a change of plate current of 1 milliampere, the mutual conductance

$$G_m = \frac{1 \times 10^{-3}}{1} = 1 \times 10^{-3} \text{ mho or } 1000 \text{ micromhos.}$$

The mutual conductance is defined, too, by the ratio between the amplification factor and the plate resistance. Thus

$$G_m = \frac{dI_p}{dE_g} = \frac{\mu}{R_p} \text{ because } \mu = \frac{dE_p}{dE_g} \text{ and } R_p = \frac{dE_p}{dI_p}.$$

$$\text{Therefore } \frac{\mu}{R_p} = \frac{\frac{dE_p}{dE_g}}{\frac{dE_p}{dI_p}} = \frac{dI_p}{dE_g}.$$

Problem 8–9. A tube has a plate current of 7.75 ma. at zero grid bias and 3.8 ma. at $E_g = -4$. What is the mutual conductance?

Problem 9–9. The mutual conductance of a tube is 800 micromhos. What change in plate current is produced by a 1 volt change on the grid?

Problem 10–9. The mutual conductance of a tube is 775 micromhos. The plate current at $E_g = -6$ is 2 ma. What is the plate current at $E_g = -2$?

156. Importance of mutual conductance.—The tube is ordinarily so worked that small variations in input (grid circuit) a.-c. voltage produce variations in output (plate circuit) a.-c. currents, and it is important that the mutual conductances of a tube shall be high. Tubes are in general use which have amplification factors as low as 3 and as high as 30, the plate resistance ranging from 2000 to 100,000 ohms. When still greater amplification constants are desired—we are speaking of small receiving tubes only—it is necessary to change the construction of the tube. It is here that the screen-grid, or four-element tube, arrives on the scene. It is described in Section 170.

When one is considering two tubes of the same type, say two 201–A tubes, the one with the higher mutual conductance is the better, but rather large differences in mutual conductance must occur before any difference in the operation of a circuit in which the two tubes are to be used will be noted. If one is to compare a CX–301–A with a CX–220 he will see that the mutual conductance of the latter is less than of the former, and yet the CX–301–A is capable of furnishing only about one-half as much undistorted power to a loud speaker as the latter. In comparing tubes of the same type which are to be used for the same purpose the mutual conductance is the best single factor—but it must not be worked too hard.

157. Slopes of characteristic curves as tube constants.—Since the plate resistance of the tube is defined as

$$R_p = \frac{dE_p}{dI_p}$$

and the mutual conductance as

$$G_m = \frac{dI_p}{dE_g},$$

these values may be taken directly from the curves showing the relation between plate voltage and plate current and between grid voltage and plate current; the reciprocal of the plate resistance is the slope or steepness of the E_p–I_p line, that is, $\frac{1}{R_p}$ = slope of the

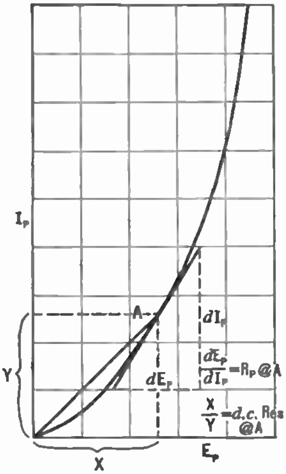


Fig. 123.—Note how R_p is obtained. It is not E_p divided by I_p, which gives the d.-c. resistance.

E_p–I_p curve; the mutual conductance is the slope of the E_g–I_p line. When changing the grid voltage produces no change in plate current (saturation) the mutual conductance is zero, that is, the E_g–I_p curve no longer has any slope or "steepness" and it flattens out, as for high positive values of grid bias. On the other hand, when the E_p–I_p curve flattens out the plate resistance becomes infinite—and so the steeper the E_p–I_p curve the lower the plate resistance. Care should be taken that the plate resistance is obtained properly from the E_p–I_p curve. Figure 123 shows the correct and incorrect methods.

Experiment 5–9. From the curves plotted in Experiments 4 and 5 measure the slopes at various values of E_p and E_g and calculate the plate resistance, mutual conductance, and amplification factor. Plot these values against grid voltage for one curve and against plate voltage for another curve. Such data for a typical tube are shown in Fig. 124.

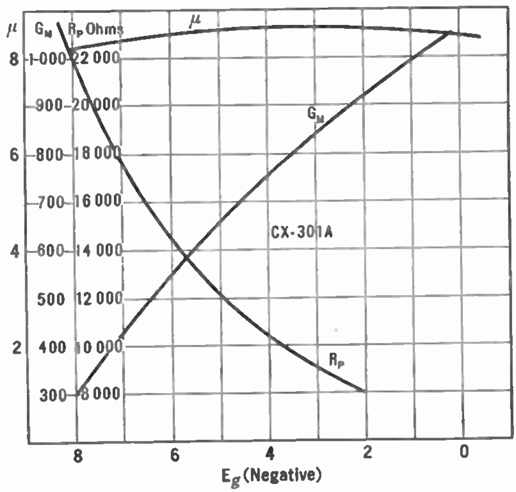


Fig. 124.—Effect of grid voltage on tube characteristics.

158. "Lumped" voltage on a tube.—An expression in England for the voltage on the plate of a tube is very useful. It involves the expression,

$$E = E_p + \mu E_g,$$

where E = the effective or "lumped" voltage on the plate;
E_p = the plate voltage due to the B battery;
E_g = the voltage on the grid, due a C bias;
μ = the amplification factor of the tube.

For example we know that adding a negative C bias to a tube's grid reduces the plate current. The same value of plate current may be attained without the C bias by reducing the plate voltage. Then for every value of plate current there is a combination of grid bias and plate voltage that will produce it, the actual values being given by the above expression.

If, then, we plot the single curve showing the plate current at various plate voltages but with the grid at zero bias, we can easily calculate what the plate current will be under some other condition of B and C voltage. Thus with zero bias and 90 volts on the plate, the plate current may be 10 ma. That is,

$$E = 90 + \mu \times 0 = 90$$

Now suppose $\mu = 8$ and $E_g = -3$

$$E = 90 + 8 \times (-3) = 90 - 24 = 66.$$

To get I_p, it is only necessary to look at our E_p–I_p curve for $E_g = 0$ and find what I_p is when $E_p = 66$. This is the value of current desired, and is one point on the new curve $E_g = -3$. Then assume some other value of E_p and find the new I_p and place a mark on the graph paper for this point which is the second for the $E_g = -3$ curve. Other points may be obtained for other values of E_p and E_g and thus any number of curves drawn which will be parallel to the first or $E_g = 0$ curve.

Problem 11–9. The μ of a tube is 3; what is the lumped or effective plate voltage when $E_p = 180$ and $E_g = -40$?

Problem 12–9. The plate voltage E_p on a tube is 120 but the plate current corresponds to a plate voltage of 40 at zero grid bias. If the value of E_g is 10, what is the μ of the tube? Do you see a simple way of measuring the amplification factor of a tube by this method?

Problem 13–9. If the plate current of a tube is 2 ma. when $E_p = 90$ and $E_g = -4.5$ and $\mu = 8$, at what value of E_p will it be equal to 2 ma. when $E_g = 0$?

159. Measurements of vacuum tube constants.—The various factors which define all of a tube's characteristics—μ, R_p, and G_m—are known as the **tube constants.** It is very important that means be handy for measuring these constants at various values of plate and grid voltage so that a full knowledge of a tube's characteristics may be had.

Such calculations may be made by means of the characteristic curves. This is slow work, however, and the experimenter or radio service man has no time for such processes. A simpler method will be described.

(*a*) *To measure the plate resistance of a tube.*

This is the ratio between the change in plate voltage and the change in plate current: dE_p/dI_p. Set the grid bias at the value desired (for example $-$ 4.5 for a 201–A tube) and choose the plate voltage at which the tube will probably operate (that is, 90 volts for a 201–A, 135 for a 112, etc.). Then fix the plate voltage at a value somewhat higher than this and read the plate current. Reduce the plate voltage to a value lower than that at which the tube is to be used and read the plate current. Suppose we are to test a 201–A type tube. The proper values are 90 for E_p and $-$ 4.5 for E_g. Set the grid voltage at $-$ 4.5 and the plate voltage at 100 and then at 80. Set down the data as below, in which the estimated currents are respectively 3 and 1 milliampere:

$$R_p = \frac{dE_p}{dI_p} = \frac{100 - 80}{.003 - .001} = \frac{20}{.002} = 10{,}000 \text{ ohms.}$$

This means that at a grid bias of $E_g = -$ 4.5, the average plate resistance between the values of E_p = 80 and 100 volts is 10,000 ohms.

(*b*) *To measure the mutual conductance.*

This is the ratio between plate current change dI_p and the grid voltage change dE_g that produced it. Set the plate voltage at the value at which the tube will operate, for example: 90 volts. If the bias under operating conditions is to be 4.5 volts (CX–301–A) set the grid at minus 5 and then minus 4 and read the plate currents. Set down the data as follows, assuming the plate currents are respectively 3 and 2 milliamperes:

$$G_m = \frac{dI_p}{dE_g} = \frac{.003 - .002}{5 - 4} = \frac{.001}{1} = .001 \text{ mho} = 1000 \text{ micromhos.}$$

(c) *To measure the amplification constant.*

The value of the amplification constant may be calculated directly from the results obtained in (a) and (b) above. Since

$$G_m = \frac{\mu}{R_p}$$

or

$$\mu = G_m \times R_p,$$

it is only necessary to multiply the plate resistance by the mutual conductance. Thus if

$$R_p = 10{,}000 \text{ ohms}$$
$$G_m = 1000 \times 10^{-6} \text{ mhos}$$
$$\mu = 1000 \times 10^{-6} \times 10{,}000 = 10.$$

The amplification constant may be determined in the following manner, which makes it unnecessary to determine first the mutual conductance and the plate resistance.

Set the plate voltage at a certain value, say E_{p_1}, read the plate current, I_{p_1}; change the plate voltage to E_{p_2}, note plate current I_{p_2}. Then bring the current I_{p_2} back to its original value I_{p_1} by varying the grid voltage. The ratio of the corresponding plate and grid voltage changes is the amplification constant, as indicated in Section 150. That is

$$\mu = \frac{E_{p_1} - E_{p_2}}{E_{g_2} - E_{g_1}}.$$

160. Bridge methods of determining the tube factors.—A number of meters have been devised to measure the three tube constants by the methods outlined above—meters which read them directly and in a very simple manner. Other methods of obtaining the tube constants are in common use in laboratories. These methods involve balancing out one voltage by another.

For example let us consider the circuit in Fig. 125. An a.-c. current flowing through R_1 and R_2 in series sets up two voltages across them. The voltage $E_1 = I \times R_1$ becomes E_g and is impressed across the grid-filament input of the tube where it is amplified by the tube to appear in the plate circuit as μ times E_g. When the bridge is balanced by varying R_1 and R_2 no voltage is across the telephones and accordingly no sound is heard. At balance

$$\mu I R_1 = I R_2$$

$$\mu R_1 = R_2$$

$$\mu = \frac{R_2}{R_1}.$$

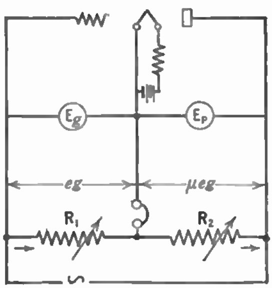


Fig. 125.—Bridge for determining amplification factor.

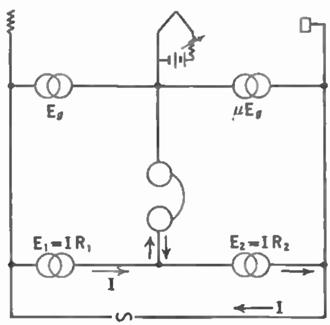


Fig. 126.—Equivalent of Fig. 125.

It is only necessary to adjust the ratio between the two resistances until the sound in the telephones is balanced out when the amplification factor is equal to the above expression. The same balance conditions may be found by substituting a battery and a key for the a.-c. voltage, and a plate current meter for the telephones. Pressing the key will change the plate current unless the ratio of R_2 to R_1 is adjusted properly. When no plate current change occurs

$$\mu = \frac{R_2}{R_1}.$$

In either of these bridges, R_1 may be fixed at 10 ohms and R_2 varied. Thus if $R_1 = 10$ ohms, and at balance $R_2 = 134$ ohms, the μ of the tube is $134 \div 10$ or 13.4.

161. To measure the plate resistance.—A bridge circuit may be set up to measure the plate resistance. There are several such bridges; one of them is shown in Fig. 127. Let us consider Fig. 128 which is equivalent to Fig. 127 (neglecting L) in which R_p represents the internal plate resistance of the tube. Current

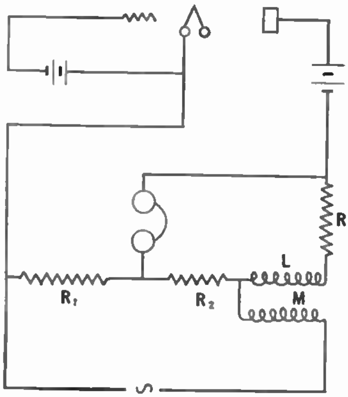


Fig. 127.—A bridge for measuring R_p.

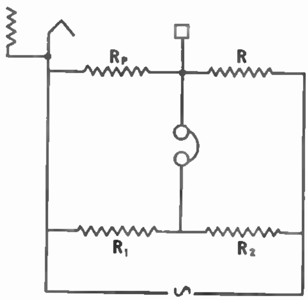


Fig. 128.—The equivalent of Fig. 127.

I from the alternator flows through R_1 and R_2 as well as through R_p and R. When no sound is heard in the telephones

$$\frac{R_p}{R_1} = \frac{R}{R_2}$$

or

$$R_p = R \times \frac{R_1}{R_2}.$$

$$\text{If } R = 10{,}000 \text{ ohms}$$

$$R_2 = 100 \text{ ohms}$$

$$R_p = 100 \times R_1$$

The inductance L is useful in balancing out certain capacity voltages. It is not necessary and its reactance can be neglected in calculating the tube constant being measured.

It is essential that small variations of voltage be used. Since the E_p–I_p curve is not straight, its slope differs at different points and is only a "constant" over a limited part of the curve. If a large variation, dE_p, is used to measure the plate resistance, or a large grid variation, dE_g, when the mutual conductance is measured the values obtained will not be very accurate. Under normal conditions the a.-c. voltages put on the grid of a tube of the 201–A type is seldom over 3 volts, and so it is absurd to measure the various constants by varying the grid more than this amount. Since the amplification factor of this tube is about 8, a grid voltage of 3 corresponds to a plate voltage variation of about 24, and so changes in plate voltage, dE_p, greater than this value should not be used when obtaining tube constants.

162. An a.-c. tube tester.—A simple tester which the diagram in Fig. 129 describes pictorially will be useful for quick tests to determine whether or not a tube should be thrown away. It comprises an a.-c. transformer which provides the proper filament voltages for standard tubes, and a resistor divided into two parts through which the plate current flows. Across this resistance appears a voltage which may be used as C bias. The operation of the tester is as follows: it is plugged into a lamp socket (a.-c. of course), the tube is inserted, and the reading of plate current noted. Then part of the grid bias resistor is shorted, thereby changing the plate current and the C bias. The ratios between the corresponding plate current changes and the grid bias changes give an indication of the mutual conductance of the tube. In actual tests it would determine the mutual conductance

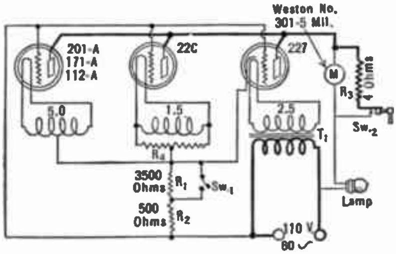


Fig. 129.—An a.-c. tube-tester.

of several types of tubes within 80 per cent or better of the value as measured upon an accurate bridge.

Suppose for example that the plate current is 0.001 ampere when the bias resistor is 4000 ohms and 0.003 ampere (3 milliamperes) when the bias resistance is reduced to 500 ohms. We set the data down as

$$G_m = \frac{dI_p}{dE_g} = \frac{.003 - .001}{.001 \times 4000 - .003 \times 500} = \frac{.002}{4.0 - 1.5} = \frac{.002}{2.5}$$

$$= .0008$$

$$= 800 \text{ micromhos.}$$

163. Types of tube filaments.—The filament of the vacuum tube has undergone many mutations since the invention of the tube. What is desired, of course, is a copious emitter of electrons, that is, one which gives off many electrons at a low filament temperature and with expenditure of little current from the heating battery. Tubes which burn with a dull glow—Western Electric tubes, the WD 12, the 112–A of R. C. A., and Cunningham, the rectifier tubes such as the UX 280, have filaments which burn at a comparatively low temperature. They are very efficient because they are coated with rare elements which emit many electrons even though the temperature is not high.

A recent type of filament is the thoriated tungsten filament. It is made of tungsten which is impregnated with atomic thorium. When the filament is heated the thorium gives off the electrons, and as the supply on the surface of the wire is exhausted a new supply comes from the interior of the filament. If, due to an accidental overload of filament voltage, the tube seems not to have the required plate current, it is probable that the balance between the rate at which the surface electrons are used up and the rate at which they come from the interior of the filament has been upset. The tube may then be reactivated, as explained in the following section.

The thoriated filament is very efficient, requiring much less power from the filament battery than any other kind of filament for a given amount of power output. The filament in the 199 type of tube is finer than the human hair, and requires only 60 milliamperes to give sufficient emission—which should be compared with the 201 type of tube used not so long ago. It then required 1 ampere at 5 volts to heat it sufficiently to give off a rather meager supply of electrons.

164. Reactivating thoriated filaments.—The older types of tube usually evidence the end of their useful life by burning out. The thoriated filament, on the other hand, has a practically constant output until the thorium is exhausted and then the output of the tube falls off rapidly although the filament still lights and looks perfectly normal. The test for such cases is to connect grid and plate together, apply a certain voltage to these common elements and the filament, read the current, and if it falls below a certain value " reactivate."

Machines for reactivating thoriated filaments are on the market and diagrams of connections for such devices and directions may be found in the Cunningham Tube Data Book, 1927. No other type of filament can be reactivated.

165. Alternating-current tubes.—Tubes which could be heated by a.c. have long been sought by all workers in radio fields because of the greater simplicity of operation. A transformer attached to an a.-c. circuit is much less cumbersome than a storage battery which must be periodically charged. There are several reasons why we cannot run the ordinary type of tube from a.c. When ordinary battery-operated tubes are lighted by a.c. an objectionable hum results. Suppose we lighted the filament from a.c. The voltage along the filament is continually changing, part of the time one side is positive with respect to the other, and part of the time it is negative. There is a continual heating and cooling going on which cannot help but transmit some of its variations to the plate circuit.

If a centertapped resistor is placed across the filament and the plate and grid circuits are attached to the center of the filament as in Fig. 176, the hum emanating from the plate circuit is less, but the filament is too light and has too little thermal inertia to withstand the continual heating and cooling without transferring some of its variations to the plate circuit. The hum is still too great.

Suppose, however, we have a very heavy filament with a low voltage across it. It has a high thermal inertia and it is possible to get a good balance between the electromagnetic and electrostatic fields at the value of plate current desired by introducing the grid and plate circuits to the center of the filament by means of a centertapped transformer winding, or a resistor. Such is the 226 type of tube. This uses a very rugged oxide-coated filament which consumes 1.05 amperes at a voltage of 1.5. The voltage drop across the tube is low, its thermal inertia is high, it has a very low hum output. It can be used as a radio-frequency amplifier and to some extent as an audio-frequency amplifier.

166. Heater types of tubes.—The separate heater type of tube has a metal cylinder which surrounds a filament heated by alternating current. The cylinder is heated by conduction and convection from the filament proper from which it is electrically insulated. (The Arcturus 15-volt heater tube has the heater and the cylinder or emitter electrically connected.) The thermal inertia of the cylinder and the insulating material is so great that fluctuations in a.-c. voltage of the filament do not affect the plate current.

The hum appearing in the plate circuit of this tube is still less than that occasioned by the use of the 226 type. It is a general purpose tube and can be used in all positions in the receiver except the final power stage. In the usual type of heater tube there are five prongs, the additional one attached to the electron source, known as the **cathode,** which is the element to which the grid and plate circuits are connected. Less hum will be evidenced if the heater (filament) is biased by the voltage determined by experiment.

It is better to use a resistor with a variable center tap with the 226 type of tube in preference to a centertapped transformer winding. In this manner the best adjustment may be found after the tube and associated apparatus have been assembled. The use of a.-c. tubes either of the heavy filament (226) type or the separate heater type (227) requires only slightly different apparatus compared to d.-c. tubes. A typical a.-c. circuit is shown in Fig. 130.

167. Operating filaments in series.—Under ordinary circumstances vacuum tubes are operated with their filaments in parallel,

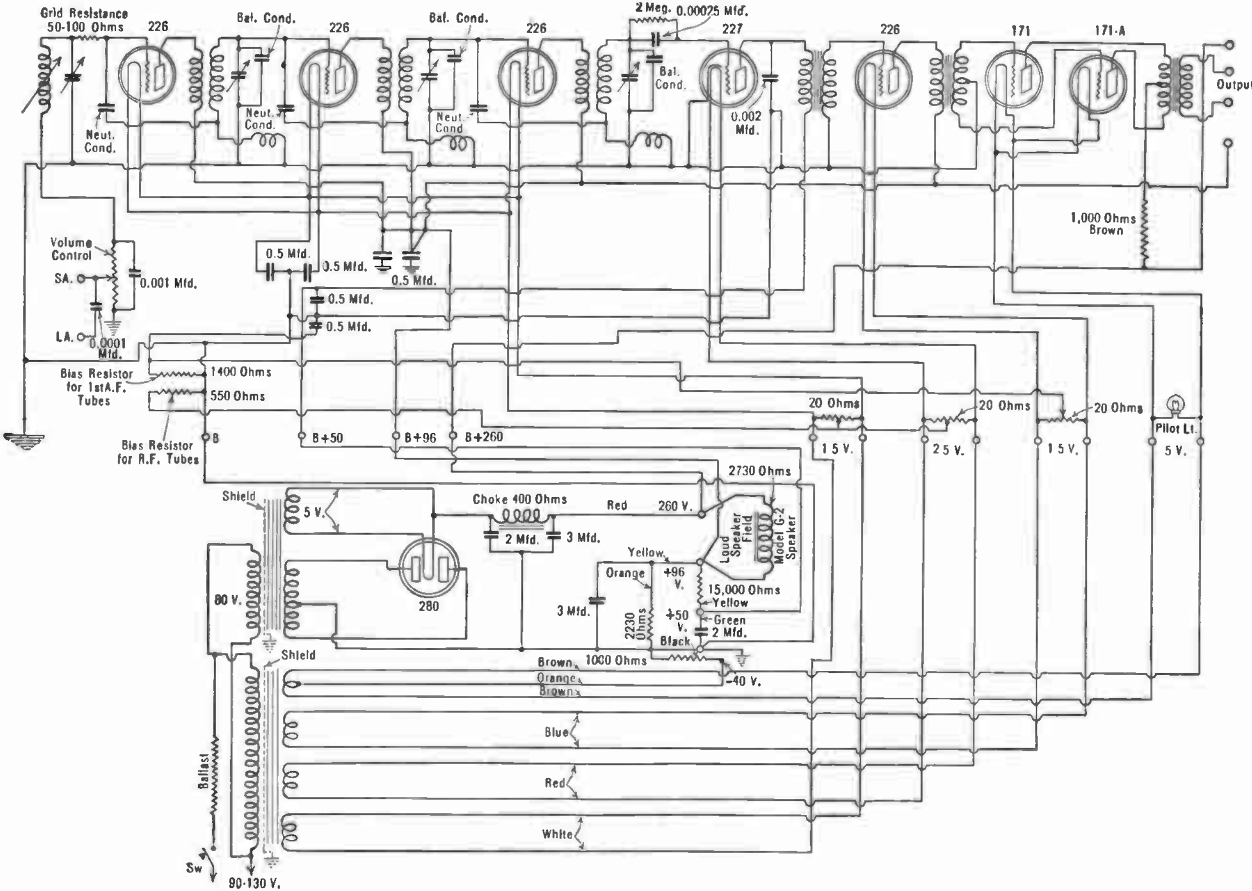


Fig. 130.—Circuit diagram of 1929 receiver—Majestic Model 70-B.

so that the total current taken is the sum of the filament currents of the individual tubes. It is possible, however, to operate the tubes with their filaments in series, and under some circumstances this is preferable to the other arrangement.

It is more difficult to rectify and filter large currents at low voltages than small currents at high voltages. If, however, it is possible to get a well rectified and filtered source of current at say 250 ma. we can operate a radio receiver with ordinary tubes from the a.-c. circuit by connecting the filaments in series.

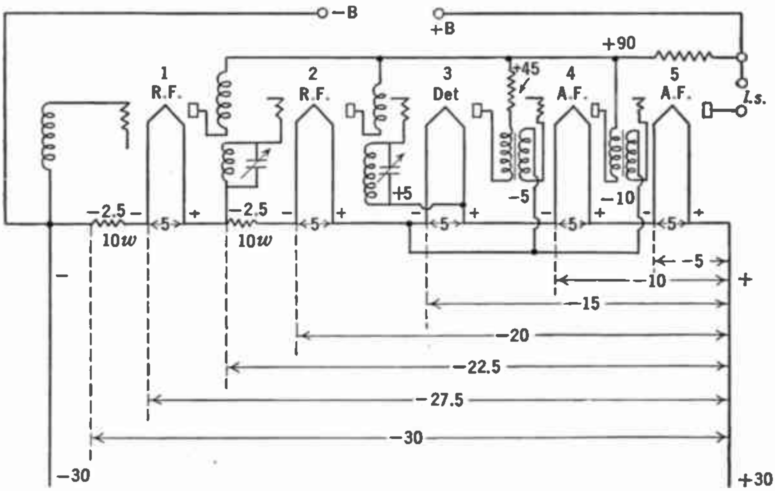


Fig. 131.—A series filament circuit in which the voltage drop across a tube's filament is used as another tube's grid bias, etc.

Let us consider the circuit of Fig. 131 in which the filaments are wired in series. In this case the same current flows through each tube and the total voltage required is the sum of the voltage drops across the tubes and the 10-ohm resistor. To operate a receiver using five 5-volt tubes requires a source of current that will produce 250 ma. at a voltage of 5 × 5 or 25 volts plus whatever additional *C* bias voltages may be necessary. The current enters one end of the filament series and exits at the other. As we go along the receiver there is a series of voltage drops, each filament as it gets farther and farther away from the positive terminal becoming more negative with respect to the preceding tubes. The drops in voltage along the line may be utilized as C bias voltages for other tubes.

For example suppose the final tube (No. 5) is a power tube requiring a C bias of 10 volts. We note that the negative terminal of the filament of tube 3 is 10 volts more negative than the negative terminal of tube 5 because there is a 5-volt drop across the filament of tube 4 and an additional drop of 5 volts across tube 3. We attach the grid circuit to this point in the circuit. If tube 4 requires only 5 volts C bias we can attach its grid circuit to the same point in the circuit because so far as tube 4 is concerned this point is only 5 volts negative. If the detector tube 3 requires a C bias of positive 5 volts we can attach its grid circuit to the positive leg of its own filament.

Suppose the first two tubes in the set do not require 5 volts bias but some value less than this. All that is necessary is to insert a resistor in the circuit ahead of that tube so that the negative drop in voltage in this resistance will be utilized. Thus in Fig. 130 the 250 ma. through a resistance of 10 ohms will produce a drop of 2.5 volts. The grid circuit should be attached as shown.

The 250-ma. supply may be a rectifier such as is used to charge storage batteries, or it may be a gaseous tube of the Raytheon type, or a chemical rectifier or some other means of rectification. The filtering is a big problem, and has limited the use of such a system. It is fairly simple, however, to get a 60-ma. current which may be used to light the filaments of 199-type tubes, and many series filament receivers have been built utilizing this scheme of connections.

168. Compensating for plate current flowing through filaments.—It should be noted that the plate current of tube 5 to return to the negative side of this tube's filament must pass through the filaments of all the other tubes. In a similar manner the plate current of tube 4 must pass through the first three tube filaments. The filament of tube 1 not only has 250 ma. (or 60 ma.) through it but the plate currents of the other tubes as well. This may cause serious overloading of the tube filament, and means must be taken to avoid this. A resistance shunted across the filaments such that the total current passing through the tube is only its normal value is one way of avoiding trouble of this kind.

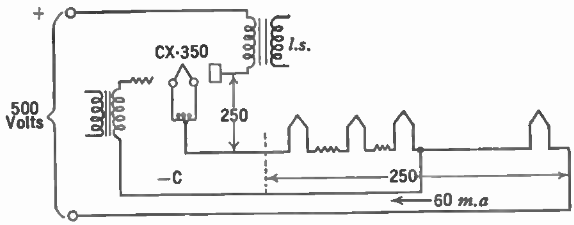


Fig. 132.—A series filament circuit in which the plate of the power tube is in series with filaments of the other tubes.

The plate of the final tube in the receiver may be connected in series with the filaments and resistors of the other tubes, as in Fig. 132, or in parallel to this string of tubes as in Fig. 133. In case the final tube takes 60 ma. of plate current its plate circuit may be in series with the filaments of the previous tubes. If this

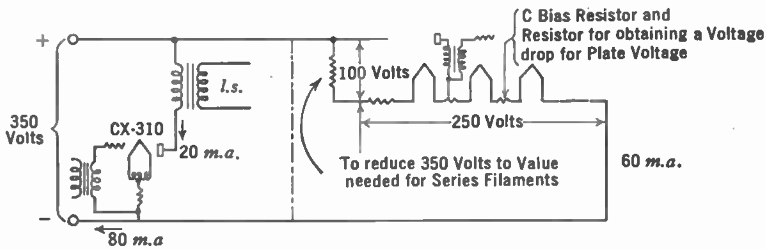


Fig. 133.—Series filament circuit in which the plate of the power tube is in parallel with the filaments of the other tubes.

final tube takes only 50 ma. of plate current, a resistance placed in parallel with the tube will increase the current to the required amount. One system requires a high voltage at a low current; the other requires a lower voltage at a higher current.

In all such systems the current must be well rectified and filtered. Because the plate current of one tube may flow through the filament of another tube, or through a resistor which is common to some other tube's grid or plate circuit, there is always danger of regeneration and unwanted couplings. These may be reduced by proper by-passing and filtering of all a.-c. circuits as described in the following chapter.

169. Means of obtaining C bias in amplifier tubes.—In all amplifiers of the present time it is desirable to maintain the grids of the tubes at a negative potential with respect to the filament. Such biasing keeps the plate current low, and if properly done will situate the operating point on such a part of the characteristic that minimum distortion due to overloading and curvature results.

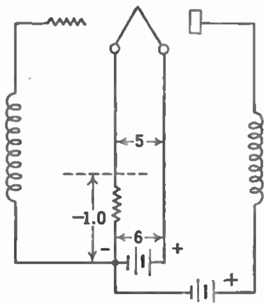


Fig. 134.—Obtaining grid bias by means of filament-current flowing through a resistance.

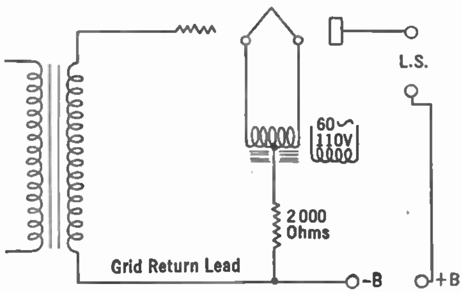


Fig. 135.—Obtaining grid bias by means of plate current flowing through a resistance.

Bias voltages may be obtained from a C battery. The voltage drop across a resistance in the tube's own filament may be used as bias, as is shown in Fig. 134. Remembering that all voltages in the circuit are reckoned either from the negative side of the filament or from the center of the filament (or the cathode in the case of heater tubes) we see that the grid of this tube is negative by the amount of the voltage drop in the resistance. Attaching the grid "return" to this point gives it a 1.0-volt bias. Another method involves using a resistance through which flows the plate current of the tube (or several tubes). Thus in Fig. 135, which represents the conventional power stage for the radio receiver, the 2000-ohm resistor is connected to the center tap of the filament transformer. The plate current flows through this resistor, producing a voltage drop there, and since the end toward the B battery is more negative than the end toward the filament, the grid return lead of that tube may be connected to the same point as the negative B lead. The grid is then biased negatively by the voltage drop in this resistor. If the plate current is 20 ma. the grid bias will be equal to .020 × 2000 = 40 volts. If because of an increase in plate voltage from any cause the plate current increases to 25 ma. the grid bias increases to 50 volts—and such a biasing scheme provides some protection for the tube. When the plate voltage changes, the grid bias changes too and tends to keep the plate current within prescribed limits.

170. Screen-grid tube.—In many uses, notably as radio-frequency amplifiers, the capacities which exist within the tube are detrimental. There are three such capacities, the grid to filament, grid to plate, and filament to plate. Because of the grid-plate capacity a path exists between the input (grid circuit) and the output (plate circuit) of the tube so that variations in the output may affect the input. Because of the amplification factor of the tube these variations may be amplified and repeated back into the plate circuit and the performance repeated until the normal functioning of the tube is seriously impaired. It would be an advantage if the grid-plate capacity of tubes could be eliminated or reduced.

Because of the space charge—the cloud of negative electrons between the filament and the plate—the current that can flow in the plate circuit is limited, and if this space charge could be eliminated, or at least reduced, the grid voltage would have a much greater controlling effect on the plate current.

Both of these beneficial effects may be secured by the screen-grid tube. In this tube, the grid-plate capacity has been reduced from an average value of 6.0 mmfd. to about 0.02 mmfd. and an amplification factor of several hundred is not difficult to attain and at the same time the plate resistance of the tube does not become prohibitively great.

The screen-grid tube consists of the usual elements and an additional grid. The second grid is maintained at a positive potential with respect to the heater or filament and thereby does away with the space charge as well as serving as a shield for the plate.

In Fig. 136 is an illustrative example of what the second grid does to the tube. If any difference of potential exists between the plates *P* and *G*, a capacity exists between them, and any a.-c. voltage attached to the system will cause an a.-c. current to flow. Now if a plate is placed between *P* and *G* and grounded, the current as read by the current meter drops to zero, because this part of the circuit has been shielded or protected from the a.-c. voltage. The capacity between *P* and *G*, then, becomes zero.

In the tube *P* and *G* are the plate and control grid respectively and the extra grid is the screening plate. It is impossible to screen the plate from the grid completely because some electrons must get to the plate through the grid, or the tube would be worthless. The screen grid is fixed at some positive potential lower than that of the plate. The fineness of this grid and its position controls the screening effect upon the plate. The electrons from the filament proceed toward the screen grid at considerable speed and most of them go through it and are collected by the plate provided it is at a higher potential than the screen. Because of the interposition of the screen grid between the plate and the control grid, the rate at which electrons go across the space is not controlled so much by the plate voltage as it is by the voltages on the two grids. In other words the plate current is more or less independent of the plate voltage, and the plate resistance—which is the ratio between changes in plate voltage and changes in plate current $\left(\frac{dE_p}{dI_p}\right)$—is very high, 750,000 ohms for the d.-c. tube (UX 222) and 400,000 ohms for the a.-c. tube (UY 224).

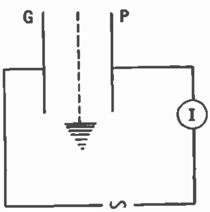


Fig. 136.—Capacity current from grid to plate is nullified by grounded shield or screen.

The mutual conductance of the a.-c. tube is about 1000 and the amplification factor is 400. It has a 2.5-volt heater type of filament.

Because of the high voltage amplification, the control grid must be protected from all other wires and circuits. It is connected only to a cap on top of the tube, and in practice is connected to its proper circuit by a wire which is covered with a grounded shield. The entire tube is also covered and thus all stray voltages are prevented from getting to the control grid. High a.-c. voltages may get to the screen grid and this circuit should be carefully filtered.

171. Characteristic curves of the screen-grid tube.—Some of the characteristic curves of the a.-c. screen-grid tube are shown in Fig. 137. It will be seen that changes of plate voltage have

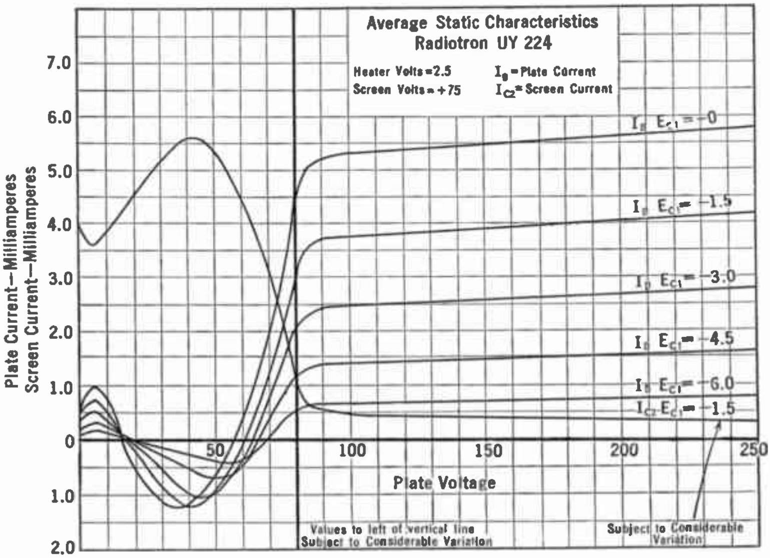


Fig. 137.—Characteristic curves of UY 224. In the region to the left of the 80-volt line there may be as much or more current flowing away from the plate as toward it, due to "secondary emission."

little effect on plate current; that at low plate voltages the current actually decreases instead of increases. At plate voltages lower than the screen grid voltage electrons may come from the plate and go to the screen grid, thereby causing the current to the plate actually to decrease. This backward-flowing circuit is due to "secondary emission." That is, an electron from the filament may get through the screen grid, but at the plate it dislodges an electron and then both are dragged back to the screen grid because of its greater positive potential.

The sum of the currents taken by the screen grid and the plate is almost constant, and is never very high. The average plate current is about one milliampere for the d.-c. tube and about 4.0 ma. for the a.-c. tube. Normal voltages are 135 to 180 on the plate and 45 to 75 on the screen grid, and minus 3.0 on the control grid.

When used as an amplifier, the tube is operated on some portion of the long almost-flat part of its plate current-plate voltage curve. Although the curved parts of the characteristic present interesting possibilities, little has been done toward utilizing them.

Early receivers utilizing screen-grid tubes suffered from many troubles. Among others was the production of cross-modulation or cross-talk by strong undesired signals. For example a receiver might be tuned to a fairly low strength station. This meant that the volume control, usually either grid or screen voltage, was turned up high so that the screen-grid amplifiers were working near their maximum sensitivity. These tubes had such a short range of grid voltage over which they could work that a strong signal would force the grid voltage to the point where the a.-c. plate current would cut off. This resulted in severe distortion, evidenced by blurbs or gasps of undesired modulation crashing through the desired program, or by hum entering from the power supply.

Late in 1930 a new screen grid tube made its appearance and became of considerable importance in the following year. This was the variable-mu or exponential tube. It had a very long, fairly flat characteristic at the bottom of its E_g–I_p curve. In other words strong negative voltages on the grid did not force the plate current to zero, and such cross-modulation due to plate current cutoff was prevented.

Because of the very long even characteristic, the tube was nicely adapted for automatic volume control, for radio and intermediate amplifiers, and for recording signal strength, or loud speaker output or other measurements where large ranges of current or voltage, etc., were to be measured.

172. Space charge grid.—If the grids in the tube are reversed, i.e., the normal screening grid is used as the signal or control grid, and the normal control grid—the one next to the filament—is made positive, the tube may be used as what is known as a **space charge grid** tube. The advantage of a much lower plate resistance and of a large amplification factor is thereby secured.

The screening effect of protecting the grid from potential variations in the plate circuit is eliminated, however, and the tube is no longer good at radio frequencies. Because of the high internal capacities in this connection, the space charge grid tube tends to discriminate against high audio tones when used as an audio amplifier.

173. Mistreatment of tubes.—Overloading the filament of a tube with higher currents than they are rated for is one of the surest methods of shortening the life of that tube. If the voltage across a tube is 10 per cent greater than normal (thoriated filaments) the life will be decreased by much more than this percentage. It is also true that the plate current should not be allowed to run higher than normal. Many receiver manufacturers in the past have used general purpose tubes without adequate *C* bias with the result that the plate current might be doubled over its normal value. This plate current must come from the filament, and flowing through the tube's resistance amounts to a certain amount of power which must be dissipated. Thus if a tube has a resistance of 20,000 ohms and a normal plate current of 2 ma., the power that must be dissipated on the plate is 0.08 watt, but if the current is permitted to become as high as 4 ma., which without *C* bias is a reasonable figure, the plate power becomes 0.32 watt—four times as great. This heat may not damage the filament, but it is certain to do it no good, and the electrons from the filament are being used at a much greater rate than is necessary or desirable. Turning up the filament voltage or increasing the plate current in order to improve the operation of a receiver is a sure sign that the receiver is poorly designed or engineered, and that a new set of tubes will be needed before long.

The vacuum tube is a delicate device and must be treated with the care one expends upon a good watch. When it is mistreated, its life is shortened.

CHAPTER X

THE TUBE AS AN AMPLIFIER

In the usual receiver, at least four of the tubes are used as amplifiers; two of them amplifying the signals at radio frequencies, two of them amplifying the voice or musical frequencies after the fifth tube has demodulated the amplified radio-frequency wave. How does the tube amplify?

174. The tube as an amplifier.—Let us look at the curve in Fig. 138 which shows in exaggerated form the relation between plate current and grid voltage. The slope of the curve, $\frac{dI_p}{dE_g}$, is the mutual conductance of the tube and tells how many milliamperes the plate current changes when the grid potential is changed one volt. The curve shows that adjusting the C bias on the grid of the tube to 5 volts, that is, placing a 5-volt battery between the grid and the most negative part of the tube filament, permits a plate current of 3 milliamperes to flow. If this bias is decreased to 4 volts, the plate current increases to 3.6 ma.; if the bias is increased to 6 volts the plate current decreases to 2.4 ma. These points on the static characteristic curve are labeled as A, B, and C.

These points are called the **operating points.** Thus when the C bias is changed the operating point slides up and down on this steep E_g–I_p curve. If this C bias is changed in some regular fashion, say in the form of a sine wave between 4 and 6 volts peak, the plate current must change accordingly, that is, it will increase and decrease between 3.6 ma. and 2.4 ma., as the curve shows The average bias is 5 volts; the average current is 3.0 ma. The maximum bias is 6 volts, the minimum is 4; the maximum current is 3.6 ma., the minimum is 2.4.

The bias may be changed in this manner by setting up an a.-c. voltage across a resistor as in Fig. 139. Suppose, as an example the voltage, E, across this resistor is a sine wave of a maximum value of one volt. When this sine wave of voltage makes the grid end of the resistor negative by one volt the actual voltage on the

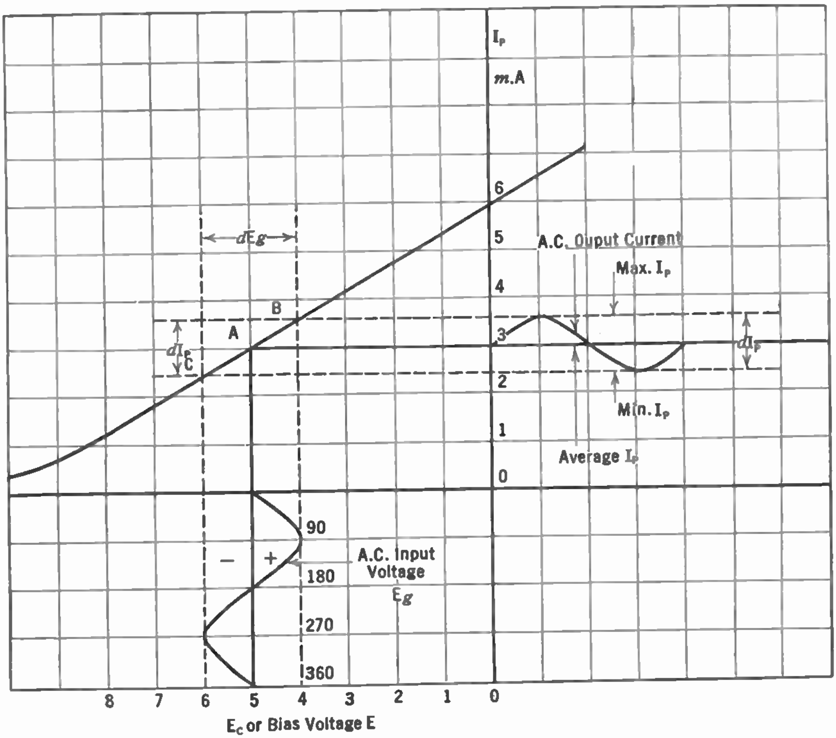


Fig. 138.—Use of straight part of characteristic. The wave form of output current will be exactly similar to the wave form of the input voltage if the characteristic is straight.

grid will be 5 volts (E_c) plus 1 volt (E) or 6 volts in all. The plate current will be, at that instant, 2.4 milliamperes. When the a.-c. voltage reverses and makes the bottom or filament side of the resistor negative, the bias on the grid is 5 volts (E_c) minus 1 volt (E) or 4 volts in all; the plate current at this instant will be 3.6

ma. At all other instants the plate current will be different depending upon the instantaneous value of the a.-c. input voltage. The plate current changes in unison with the grid voltage, and if this grid voltage varies in a sine wave there will be a sine wave of current in the plate circuit.

We can picture what happens by the sine waves in Fig. 138. With no input the grid voltage is that of the C battery, the plate current is that corresponding to this value of C bias and a plate voltage, E_p. Now let us assume that an a.-c. voltage requiring one second for a complete cycle is applied to this grid. Starting from zero it increases in a positive direction making the grid more positive (less negative) with respect to the filament. The plate current begins to rise accordingly. At the end of a quarter-second (90°) the voltage is a maximum in the positive direction and the plate current is correspondingly a maximum. Now the grid voltage begins to decrease (become more negative), the plate current decreases, and at the end of a half-second (180°) the voltage and current arrive at their original no-input values. Now the grid voltage ($E_g = E_c + E$) continues to decrease until at the three-quarter-second phase the voltage is a minimum and so is the plate current. Thereafter the voltage and current increase again and at the end of a full second are equal in value to the starting or no-signal values. Thereupon the cycle is repeated.

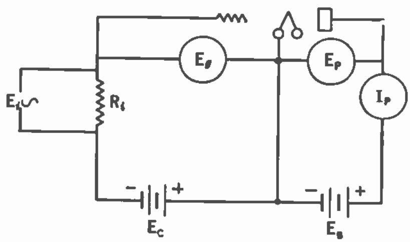


Fig. 139.—When E_i is applied, I_p consists of an a. c. current as well as steady plate current.

Notice that the two curves have the same form; that the steady bias line of 5 volts is in the exact center of the a.-c. input voltage curve; that the average plate current is the current corresponding to 5 volts negative C bias. The fact that the plate current curve seems to have less amplitude than the grid voltage variation is not important—this is a matter of the scale to which the two are drawn. One is in volts, the other is in milliamperes. This a.-c.

plate current may be thought of as a variation in the d.-c. plate current at a rate corresponding to the frequency of the input voltage, or as a true a.-c. current which flows in the plate circuit in addition to the d.-c. current.

A meter in the plate circuit of the tube would read only the average current unless its needle were capable of following the changes in current. If the input a.-c. voltage were 1000 cycles, for example, the needle would not be able to follow such rapid variations and would register only the average value of plate current, that is, the plate current corresponding to 5 volts bias or 3.0 milliamperes.

This is essentially the theory of the action of the tube as an amplifier. An input a.-c. voltage is applied to the grid. The variations in grid voltage about some average value equal to the *C* bias produce corresponding variations in plate current. These variations in current are caused to flow through some sort of output load impedance, and across this impedance they set up voltage variations. If the bias (E_c) and plate voltage E_p are properly chosen so that the variations in E_g (dE_g) take place on a straight part of the E_g–I_p curve the form of the a.-c. current wave in the plate circuit will be exactly similar to the a.-c. voltage wave on the grid. If the proper conditions of E_c, E_p, and load impedance are fulfilled, the voltage appearing across this impedance will be not only an exact replica of the a.-c. grid input voltages, but will be an amplified replica of them.

The question naturally arises, how much amplification can be obtained? What are the conditions for such maximum amplification?

175. Resistance output load.—If, in the plate circuit of the tube we put a resistance, R_o, as in Fig. 140, we may adjust conditions so that distortionless amplification results. These conditions, briefly, are: (*a*) the *C* bias and magnitude of the input a.-c. voltage must be such that only the straight part of the characteristic is used; and (*b*) the load resistance, R_o, must be large compared to the plate resistance of the tube.

Let us look at the circuit in Fig. 140 rather criticially. It is the fundamental amplifier circuit. The plate voltage, E_p, as measured by a voltmeter connected from plate to the negative filament lead is no longer the voltage across the B battery. It is less than this value by the voltage drop in the resistor R_o, i.e., the IR drop caused by the plate current. The voltage actually on the plate then is

$$E_p = E_b - I_p \times R_o \quad (1)$$

If, for example, the B battery voltage = 180 volts, R_o = 100,000 ohms, I_p = 0.5 milliampere, $I_p \times R_o = 0.0005 \times 100{,}000$ or 50 volts, and $E_p = 180 - 50 = 130$ volts.

Now it can be seen that any variation in I_p causes a variation in the IR drop across R_o, and hence the plate voltage E_p must change according to equation (1). For this reason any variation in the grid bias will cause a variation, not only in the plate current of the tube but a variation in the plate voltage as well. We cannot use the static characteristic to determine what the output voltage looks like, because the plate voltage is no longer constant, but changes in instantaneous value with each instantaneous value of the grid voltage. The operating point, then, does not slide up and down the characteristic curve as plotted in Fig. 138 but along a new kind of curve known as a **dynamic** characteristic curve.

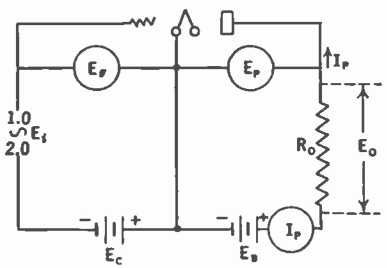


Fig. 140.—Ratio of E_o to E_i is the voltage amplication of circuit.

176. Dynamic characteristic curves.—A series of dynamic curves is shown in Fig. 141. They were taken by placing resistances in series with the plate battery and a 171 power tube maintaining the voltage on the plate equal to 180 when the C bias was 38.5. It will be noted that they are much flatter and longer than the static curves. This means that plate current variations are much smaller in magnitude under the same grid voltage variations. The mutual conductance of the circuit is no longer as high as the value for the tube alone—but the slope of the curve tells us the a.-c. current which will flow through the resistor when a given a.-c. voltage is applied to the grid, and these curves are therefore more useful than the static curves.

Experiment 1–10. Connect as in Fig. 140 a tube of the 201-A type, a plate battery, and a resistance. Short-circuit terminals for E_i. Measure and plot the current in the plate circuit as the grid voltage is varied. Then change the resistor and repeat. Use values of 8,000, 16,000, 24,000 and 48,000 ohms.

177. Phase of E_g, E_p, and I_p.—When the grid of the tube is made negative the plate current decreases; when the grid is made

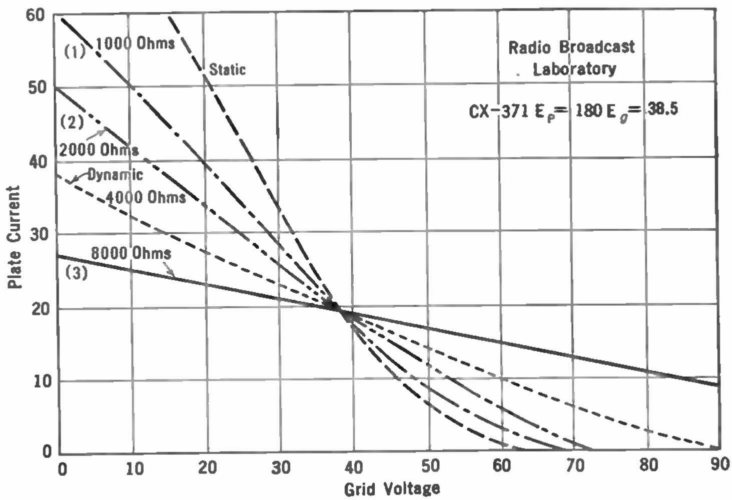


Fig. 141.—Dynamic characteristic curves.

less negative the plate current increases. When the plate current increases, however, the voltage drop, IR_o, across the resistor, R_o, increases and for this reason the voltage E_p actually on the plate decreases. That is, the plate current increases when the grid voltage increases (becomes less negative), but on the contrary the plate voltage decreases when the grid voltage increases. Thus we may say that the plate current variations are in phase with the grid voltage variations whereas the plate voltage variations are out of phase with the grid circuit variations. These phase relations are shown in Fig. 142.

178. Magnitude of the amplified voltage.—There are several variable factors in a one-stage resistance-coupled amplifier, as shown in Fig. 140. The grid bias, E_c, the battery voltage, E_b, the

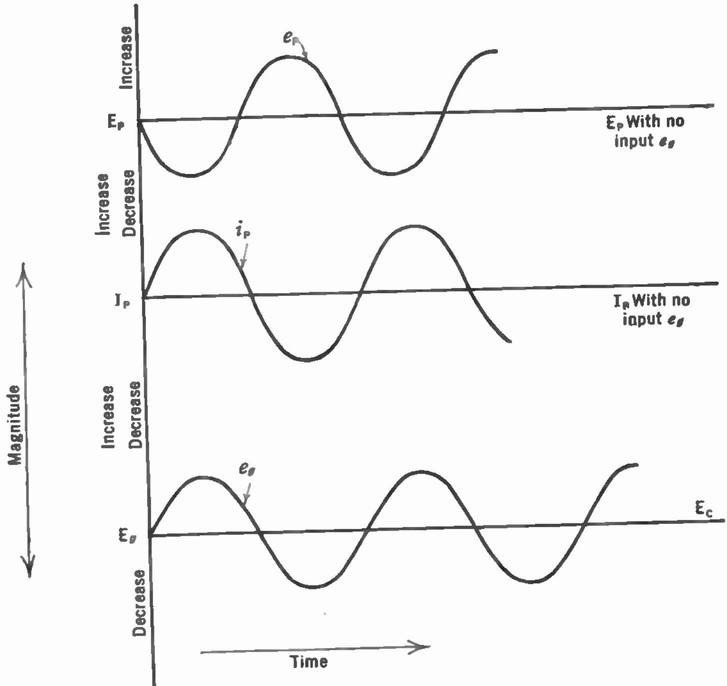


Fig. 142.—Phase relations between a.-c. grid and plate voltage and plate current.

load resistance, R_o, all may be changed as desired. With a fixed value of E_c and E_b, the plate resistance of the tube, R_p, is fixed. If we go into the laboratory and measure the voltage across a load resistance with a given value of a.-c. voltage on the grid we shall determine the voltage amplification of the stage. Then if we change the load resistance and measure the output voltage across R we shall get a curve which shows that the amplification increases as the load resistance increases, but finally comes very near a certain fixed value—which is numerically equal to the amplification factor of the tube—and that increasing the load resistance beyond this point has little effect on the amplification.

Because each change in R_o will change the plate current, we must adjust the plate battery each time so that the voltage actually on the plate—which is E_b minus the voltage drop along the load resistance—is the same.

The amplification that will be realized in a laboratory experiment of this kind may be calculated from this formula

$$\frac{\mu R_o}{R_o + R_p} = G \text{ (voltage amplification)} \tag{2}$$

and the r.m.s. a.-c. plate current from

$$\frac{\mu e_g}{R_o + R_p} = i_p \tag{3}$$

and the r.m.s. a.-c. voltage across the load from

$$\frac{\mu e_g R_o}{R_o + R_p} = Ge_g = e_o, \tag{4}$$

where e_g = r.m.s. grid voltage.

179. Equivalent tube circuit.—These same voltages and currents can be obtained from the circuit in Fig. 143 by simple Ohm's law calculations. For this reason it is standard practice to substitute for the tube its equivalent consisting of a voltage μE_g in series with two resistances, one equal to R_p, the tube resistance, and the other, R_o, equal to load resistance.

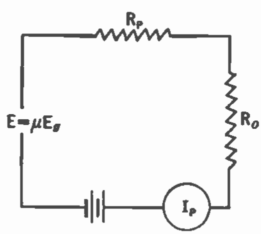


Fig. 143.—Equivalent circuit of amplifier tube.

The maximum voltage amplification takes place when the external resistance, R_o, is infinite. Practically, however, 75 per cent of the maximum amplification is obtained when R_o is 3 times as great as R_p. For example, if R_p is 10,000 ohms, a coupling resistance of 30,000 ohms will realize 75 per cent of the μ of the tube. The maximum possible value is the amplification factor of the tube. Thus if a tube especially made for resistance-coupled amplifiers having an amplification factor of 30 is used, the maximum possible amplification will be 30, but under actual operating conditions the voltage amplification, K, of the complete circuit is about 20.

180. Power output.—The a.-c. power in the load resistance is calculated as follows,

$$P = i_p^2 R_o$$

$$i_p = \frac{\mu e_g}{R_o + R_p}$$

$$P = \frac{(\mu e_g)^2 R_o}{(R_o + R_p)^2} \qquad (5)$$

This is a maximum when the two resistances are equal, that is, when

$$R_p = R_o$$

Then the power

$$P = \frac{\mu^2 e_g^2}{4R_p} \qquad (6)$$

where e_g = r.m.s. input voltage;
and

$$P = \frac{\mu^2 E_g^2}{8R_p} \qquad (7)$$

where E_g = peak or maximum input voltage.

This power which is fed into the load resistance must come from the plate battery, because the tube itself generates no power —it acts merely as a transformer or valve which takes small voltages and currents on its input and turns out larger voltages and currents to its output circuit. The power in the input circuit must come from the circuit to which the tube is attached. The power in the output must come from the batteries. The tube therefore releases power from the batteries in a form which is an exact replica of the power utilized in the input circuit to which the tube is attached.

181. Power amplification.—Ordinarily the grid of a tube is biased so highly negatively that practically no current flows in the grid circuit. The tube input circuit itself then draws little or no power. If, however, the a.-c. voltages are fed into the tube through a resistance, some power is expended in this input resistance. If the values of resistance and current are known the power may be calculated. The power amplification will be the output power divided by the input power. The fact that a tube is a power multiplier distinguishes it from a transformer which is merely a power transmitter, taking power at one current and voltage and passing it on at another current and voltage. The transmitted power is never more than or even equal to the input power. It is always less; unlike a tube, the transformer cannot amplify power or release it from local batteries. The power output is proportional to the square of the voltage on the grid. Thus doubling the input a.-c. voltage quadruples the output a.-c. power.

Example 1–10. Four milliamperes of current at 1000 cycles are fed through a 10,000-ohm resistance in series with the grid of a tube and its C battery. In the output is a 2000-ohm resistor. The amplification factor of the tube is 3, its internal plate resistance is 2000 ohms. What is the power output, what is the voltage across the output, what is the voltage and power amplification, and what power is lost on the internal resistance of the tube?

Let the input voltage $E_i = I_iR_i = .004 \times 10{,}000 = 40$ volts r.m.s.

$$\text{voltage amplification } G = \frac{\mu R_o}{R_o + R_p}$$

$$= \frac{3 \times 2000}{4000} = 1.5 \text{ times.}$$

The output voltage $E_o = E_i \times G = 40 \times 1.5 = 60$ volts r.m.s.

$$\text{Power output } P_o = \frac{\mu^2 E_i^2}{4R_p}$$

$$= \frac{9 \times 40^2}{4 \times 2000} = 1.80 \text{ watts}$$

Power input P_i $\quad I_i^2R_i = (.004)^2 \times 10{,}000$

$= 16 \times 10^{-6} \times 10{,}000$

$= .16$ watt

Power amplification $= P_o/P_i = 1.8/.16 = 11.25$ times.

Since I_p (a.c.) flows through both R_o and R_p and since $R_p = R_o$ a.-c. power lost in R_p = power lost in R_o = 1.8 watts.

Total power taken from batteries = 3.6 watts.

$$\text{Efficiency} = \frac{\text{useful power}}{\text{total power}} = \frac{1.8}{3.6} = 50 \text{ per cent.}$$

Problem 1–10. Assume a 201-A tube with a load resistance of 12,000 ohms and an a.-c. grid voltage of 3 volts (peak). The μ of the tube is 8, its R_p is 12,000 ohms. What is the maximum value of the a.-c. plate current? (Use formula 3.) What is the r.m.s. value? What a.-c. power is developed in the load resistance? What voltage appears there?

Problem 2–10. What is the voltage amplification in the above circuit? (Use formula 2.) How much would it be increased if the load resistance were increased to 36,000 ohms? How much would this change the power output?

Problem 3–10. The plate resistance of a certain "high μ" tube is 60,000 ohms and its amplification factor is 20. What plate resistor value in ohms must be used to realize a voltage amplification of 15?

Problem 4–10. A 112-type tube has an internal plate resistance of 5000 ohms, its amplification factor is 8; it is worked into a load of 5000 ohms. Plot the output power in the load resistance as the input a.-c. voltage is increased from 1 to 8 volts (peak). (Use formula 7.)

Problem 5–10. What is the voltage amplication in Problem 4.

Problem 6–10. The power output of a tube when worked into a load whose resistance is equal to the tube resistance (when the input grid voltages are maximum volts) may be written as $\frac{\mu^2}{8\,R_p} \times E_g^2$. If we divide this expression by E_g^2 we shall have a figure which gives us the power output in watts per (volt input)^2. Make a table of such values for all the tubes used at the present time, getting the tube data from the tube chart.

Problem 7–10. The normal C bias for a 112-type tube is 9 volts. What is the largest r.m.s. voltage that may be applied to its grid before the grid goes positive?

182. Amplifier overloading.—The conditions for undistorted amplification are: (a) the C bias and magnitude of the a.-c. input voltage must be such that only the straight part of the tube's characteristic is used, and (b) the load resistance must be large with respect to the internal resistance of the tube, R_p. Let us examine these conditions. Suppose first that the C bias is too great, as in Fig. 144, so that the operating point goes into a curved part of the characteristic. The wave of plate current is no longer similar to that of the grid voltage, and its average value is no longer equal

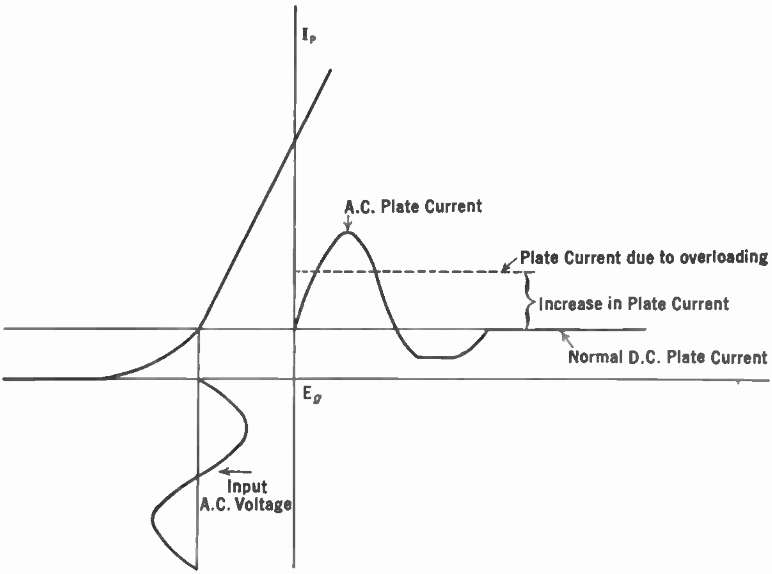


Fig. 144.—Effect of using curved part of characteristic. Note dissimilarity between output and input.

to the zero a.-c. input condition as is true when the bias is such that input voltages carry the grid operating point only over a straight part of the curve. The negative parts of the a.-c. waves are partly cut off. Distortion results because the negative and positive halves of the cycle are not amplified alike. A meter in the plate circuit would show an increase in current when signals were put on the grid—an infallible sign of overloading distortion. If the C bias is great enough and input signals are strong enough the grid may be forced so far negative that the plate current may be reduced to zero on the negative halves of the wave. This would produce even worse distortion.

Overloading, then, is a technical name for operating a tube under a wrong *C* bias, or with too strong input signals.

If the *C* bias is too small, input signals force the grid positive at times and distortion again occurs for a reason explained in Section 185. In this case the plate current as read by a d.-c. meter would decrease when the input voltages are applied to the grid.

Suppose, however, the tube is biased properly, say at the center of the region between the lower bend of the E_g-I_p curve and the point which corresponds to zero grid voltage. Distortion does not occur unless too great a.-c. voltages are put on the grid—voltages sufficient to drive the operating point down on the curve, or up on the positive part of the curve.

There are two possible remedies for such kinds of distortion. One (*a*) is to reduce the input voltage until the operating point moves over only a straight portion of the curve; another (*b*) is to increase the B and C voltages until a longer straight portion is available. As shown in Fig. 118, increasing the plate voltage moves the E_g-I_p curve to the left and increases its straight part. The *C* bias would be increased accordingly.

If the tube is properly biased, the input a.-c. voltage must be such that its peak value does not exceed the value of the *C* bias voltage. Thus if a tube has a bias of 40.5 volts, the input value of the a.-c. voltage must not exceed this value, and thus its r.m.s. value must be not over 40.5 ÷ 1.4, or about 28.5 volts. A voltage input greater than this will force the grid positive with consequent distortion. As seen in Section 186, the peak voltage input must be even less than this value to prevent the operating point going down into this curved region.

183. Distortion due to curved characteristic.—When a load is in the plate circuit of a tube its characteristic becomes flatter and its straight part longer, but at the lower part of the curve there is still a bend and throughout the E_g-I_p graph there is considerable curvature unless the load resistance is high. Large input voltages, therefore, may cause distortion because the operating point traverses curved parts of the characteristic.

Although the maximum power output is obtained from a tube when the load resistance is equal to the internal tube resistance, the maximum *undistorted* power output is attained when the load resistance R_o is twice as great as the tube resistance, R_p. Some power is sacrificed under these conditions but, as the curve in Fig. 145 shows, the loss is not great until the output load resistance is several times the tube resistance. If the load resistance is lower

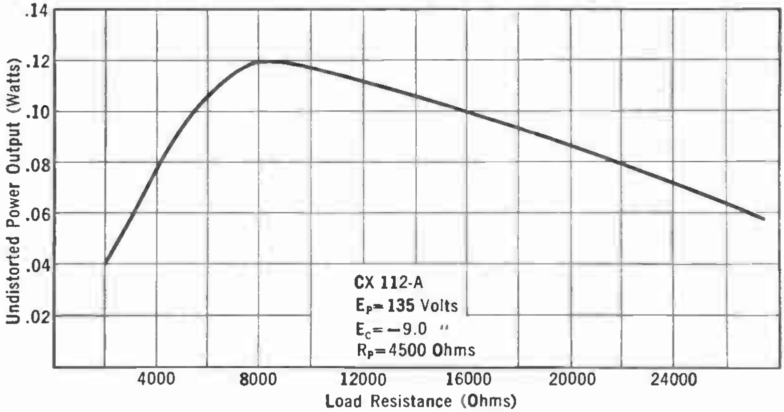


Fig. 145.—Output power as a function of load resistance.

than the tube resistance distortion due to curvature of the characeristic is bound to occur. Even with a load equal to twice the tube resistance there is considerable curvature at the bottom of the characteristic and so input voltages high enough to drive the plate current too low must not be applied. See Section 186. The power output when $R_o = 2\ R_p$ is

$$P = \frac{2}{9} \times \frac{\mu^2 e_g{}^2}{R_p}. \tag{8}$$

Distortion frequently occurs at low audio frequencies. There are two reasons for this. In the first place the excursions of the operating point may be somewhat greater on these frequencies because of the greater power in them than in high tones. In the second place, the loud speaker may have a resistance which varies with frequency, becoming low at low frequencies, probably lower than the tube resistance. Thus distortion due to curvature as well as loading distortion may occur on low notes.

The solution is to use a power tube which will easily handle the greatest input grid voltages that will be encountered, and secondly, to use a power tube with a low internal resistance so that the load resistance will, at the lowest frequency, be larger than the tube resistance.

184. Permissible grid swing.—The expression "grid swing" is often used, especially in England, to indicate the extent to which the voltage of the grid varies under the incoming signals. To state that the grid swing on a certain tube is 10 volts means that the voltage of the grid varies between 5 above and 5 below some fixed value, a total swing of 10 volts. In this country we should say the maximum input voltage was 5. Under these conditions the *C* bias should be 5 volts at least, preferably more. The maximum permissible grid swing is the range of voltage on the grid which will not cause distortion either because of the grid going positive or because of the operating point traversing the lower bend. Whether one says the grid swing that may be applied to a 171 power tube is 80 volts or whether he says that the peak voltage that may be applied is 40 volts is immaterial. They mean the same thing. The grid swing cannot be determined by looking at the static characteristic curve. It can be determined from the dynamic curve or as indicated in Section 186.

185. Distortion due to positive grid.—Why does distortion occur when the grid of an amplifier tube is permitted to swing positive on loud signals? If we plot the plate current against grid voltage, as the *C* bias in Fig. 139 is changed, we find that, when the grid goes positive, the plate current curve no longer is straight; it slumps off and soon becomes almost horizontal. Distortion will occur at the instant the input voltage takes the operating point up on the upper bend.

The reason for this bend is as follows. When the grid becomes positive with respect to the negative side of the filament, it begins to attract electrons to it and these electrons constitute a flow of current. Current flows in the grid circuit, and must go through the input resistance R_i. There is, then, an IR drop in the grid circuit, so that the voltage actually on the grid (E_g) is not the applied grid voltage E but this value minus the drop in the input resistance—just as the plate voltage is not the voltage of the B battery but this voltage minus the drop in the output load resistance. The greater the input voltage the more the grid goes positive, the greater the voltage drop in this resistance and the smaller the proportion of voltage that is actually on the grid.

The grid must never be permitted to go positive in ordinary circuits. Some circuits have been developed in which the grid is not only permitted to go positive but is forced to do so with a consequent greater power output. Such circuits are not, as yet, in general use.

186. Amount of distortion caused by overloading.—What is the result of operating amplifier tubes over a curved part of the characteristic? The result is an output wave form quite different from the input wave. Distortion is taking place whenever the magnified output voltage is not exactly, in all respects, like the input voltage. When the d.-c. plate current of an amplifier tube changes under the action of an input a.-c. grid voltage, distortion is taking place; the form of the wave in the output circuit does not look like the form of the input wave. This output wave may be very complex.

When a tube distorts, it adds certain frequencies to the output circuit which were not present in the input. All of these frequencies added together at any instant produce a wave form which looks unlike the original wave form.

How can we tell the amount of distortion to be expected with given tube and circuit constants? It is not difficult to determine what percentage of distortion will occur. Here is another place where the characteristic curves come in handy; this time the E_p-I_p curves are used.

Let us look at Fig. 146 which gives the characteristic of a Cunningham CX–371 type of tube. These data are taken from the Cunningham Tube Data Book of 1927. The vertical 180-volt line is the working line for this tube. The intersection of this line with the 40-volt grid bias line gives the plate current, 19 milliamperes. If an a.-c. voltage is placed on the grid—in addition to the 40-volt d.-c. bias voltage, of course—say of a maximum or peak value of 10 volts, the actual grid voltage will vary 10 volts up and 10 volts down from the 40-volt bias; that is, at one instant

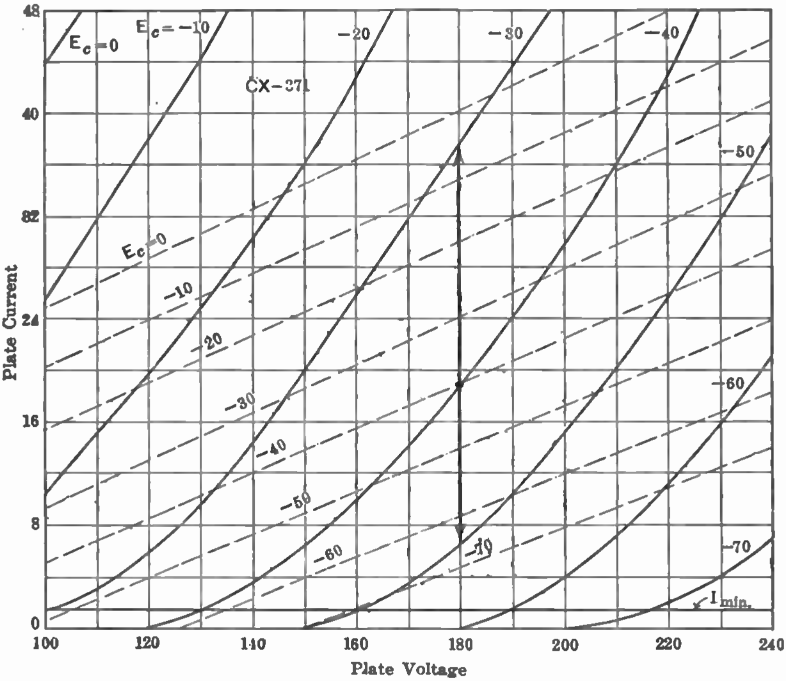


FIG. 146.—Static characteristic of power tube. Dashed lines represent characteristic with a load in the plate circuit.

it will be −30 volts and at another −50 volts. Looking at the appropriate curves in Fig. 146 we see that when the grid voltage E_c is −30 the plate current is 38 ma. and when the voltage is −50 the plate current is 6 ma. These represent changes of 19 ma. (38 − 19) and 13 ma. (19 − 6) respectively. Although the input voltage is symmetrical about the 40-volt bias voltage, the plate current is obviously not symmetrical—there is a greater change in current (19 ma.) in one direction than there is in the other (13 ma.). The output curve would not be a magnified replica of the input curve. Harmonics would appear in the output.

Now when a load resistance is placed in the plate circuit, the straight part of the curve becomes longer and flatter as shown in Fig. 141, and as more and more resistance is added the actual

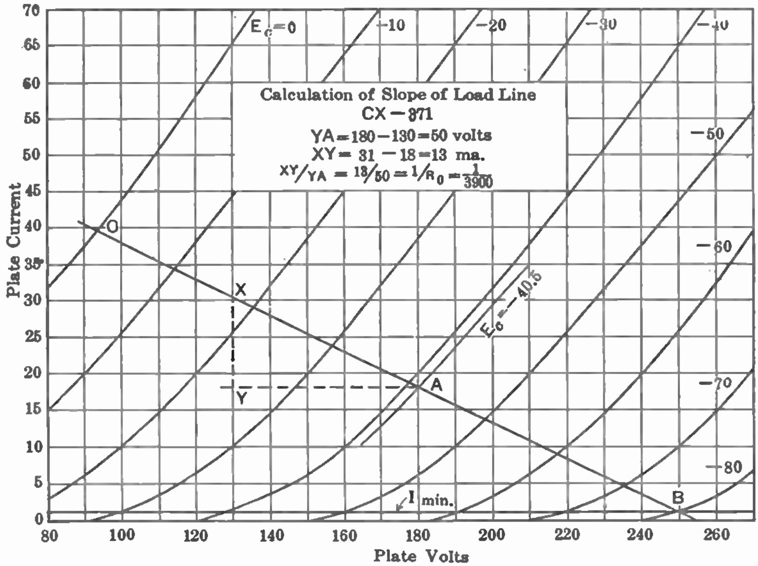


FIG. 147.—Method of plotting "load line" of a power tube. From such a curve all of an amplifier's performance can be determined.

working lines rotate about the intersection of the 180-volt plate voltage line and the grid bias line which for this curve was 38.5 volts. The plate current changes are no longer as great but they occur symmetrically about the normal plate current value which is governed by the plate voltage and the bias voltage. Thus for a given value of load resistance such that the dotted lines in Fig. 146 represent the plate current as controlled by plate and grid voltages, the same input voltage 10 (peak) causes the plate current to increase from 19 to 24 ma. in one direction and to decrease from 19 to 14 ma. in the other—a symmetrical variation.

It is a simpler process to determine the plate current variations with a given plate load resistance by the method of plotting the "load line." To do this a family of E_p–I_p curves is necessary as in Fig. 147. The load line gives the plate current at any given set of E_c and E_p values and with a given resistance load. It is determined as follows: it must pass through the intersection of the $E_p = 180$ and $E_c = -40.5$ lines, or A in the figure, because these are the recommended values for this tube, a CX–371. Through this point A draw a line parallel with the plate voltage axis. Make it any convenient length. Then at the end of this line erect a perpendicular line of such length that $YX/AY = 1000/R_o$ where R_o is the plate load resistance, in this case 3900 ohms. Through X draw a line through A and extend to the $E_c = 0$ line and the $I_p = 0$ line as in the Figure.

The reasons for this bit of apparent sleight-of-hand are as follows. The slope of this load line must be the reciprocal of the load resistance, i.e., if the load resistance, R_o, is 3900 ohms, the slope of this line must be 1/3900 ohms. The slope of the line will be equal to the vertical side of a triangle divided by the horizontal side of this triangle which has for the third side either the load line, or a shorter line parallel to the load line.

Thus, slope of load line:

$$\frac{\text{vertical}}{\text{horizontal}} = \frac{1}{R_o} = \frac{I\text{(amps.)}}{E\text{ (volts)}} = \frac{I \times 1000\text{ ma.}}{E\text{ volts}}$$

The value of plate current corresponding to any set of E_p and E_c values with this particular load resistance may be found from this line. Thus with $E_c = 0$ and $E_p = 92$ volts, $I_p = 39$ ma., with $E_c = -60$ and $E_p = 218$, $I_p = 9$ ma. Thus if the bias voltage is 40.5 and the peak voltage applied to the grid is 10, the actual grid voltage varies from $40.5 - 10$ or 30.5 to $40.5 + 10$ or 50.5 and the corresponding plate currents will be 24 and 13 approximately, or approximately 5.5 ma. up and down from the 18.5 ma. value.

Now the grid must not go positive, and the plate
not become so low on strong signals that the curved p
characteristic is used. Thus 1.0 ma. is about the lowest
current should go, or the value when $E_c = -80$. From
to -80 is 39.5 volts which is the peak a.c. that should be
the grid. This input will cause the plate current to vary b
39 ma. and 1 ma.

187. Power output calculation.—The power output m
calculated from the above data by means of the following form

$$\begin{aligned} P &= 1/8\,(E\text{ max.} - E\text{ min.}) \times (I_p\text{ max.} - I_p\text{ min.}) \\ &= 1/8\,(250 - 92) \times (.039 - .001) \\ &= .75\text{ watt} = 750\text{ milliwatts of output power.} \end{aligned}$$

188. Harmonic distortion calculation.—The amount of distortion present in such an amplifier working under such conditions may be found from the following equation in which $I_o = 18.5$ ma. which is equal to the plate current when 180 volts are on the plate and the C bias is 40.5 volts.

$$\begin{aligned} \text{Distortion} &= \frac{\frac{1}{2}\,(I_p\text{ max.} + I_p\text{ min.}) - I_o}{(I_p\text{ max.} - I_p\text{ min.})} \\ &= \frac{\frac{1}{2}\,(.039 + .001) - .0185}{.039 - .001} \\ &= \frac{.02 - .0185}{.038} = .039 \\ &= 3.9\text{ per cent.} \end{aligned}$$

This distortion is the amount of second harmonic current in the output. Thus if the input a.-c. grid voltage has a frequency of 1000 cycles and if the output current is 10 milliamperes (fundamental) there will be in the plate circuit 3.9 per cent of this current or about 0.4 milliampere in the form of a 2000-cycle wave.

It has been determined that a 5 per cent distortion is not objectionable to the ear—but this involves a matter of opinion and other factors. If and when better loud speakers are available it is possible that the average car will detect less distortion than this.

Power diagrams.—To review the tube with a resistance power amplifier, and to gather a few additional facts, let of the E_p–I_p curves as shown in Fig. 148, which is a purely etical case—the curves and values of current and voltage resent no particular tube now available; they were chosen at andom. Let us assume that the voltage actually on the plate is 160 volts when the steady plate current is 20 ma. That is, $E_p = 160$, and $I_p = 20$ ma. Let us assume a load of 5000 ohms, find

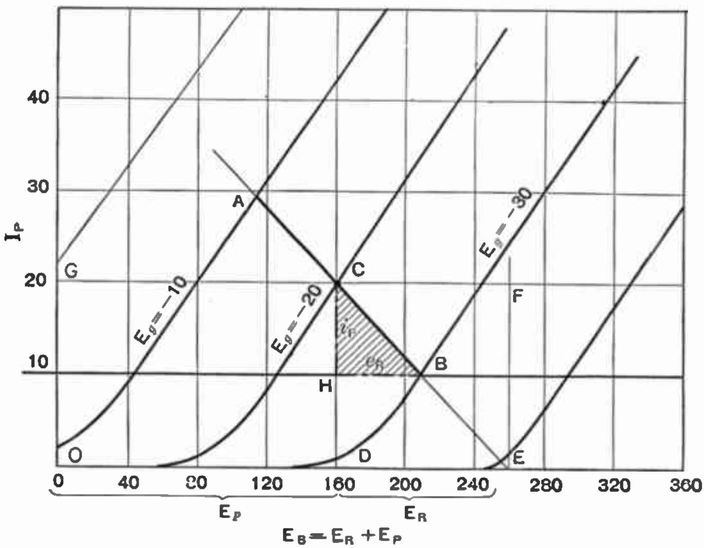


Fig. 148.—Power diagram. The area of shaded triangle represents a.-c. power used in load.

the slope, and draw the load line through the intersection of the I_p = 20-ma. line with the E_p = 160-volt line, and find that the bias on the grid to maintain such a plate current is 20 volts. Let us assume that a sine wave is put on the grid whose maximum value is 10 volts, so that the actual grid voltage varies between − 10 and − 30 volts. The corresponding I_p variations are from 30 to 10 milliamperes.

We note that the load line crosses the battery voltage line at about 260 volts. This, then, is the battery voltage necessary to insure that the plate of the tube gets its 160 volts. In other words there is a drop of 100 volts (5000 × .02) in the resistance of the load, R. Under normal conditions of no a.-c. input to the grid, the voltage across the tube is 160 volts, across the load is 100 volts, and the plate current is 20 ma.

Now the d.-c. power lost in the load is the product of the voltage across the resistance R and the current through it; and the power lost on the plate of the tube is the product of the voltage across the tube and the current flowing. Thus,

$$\text{Power lost in load} = E_R \times I_p = DE \times CD$$
$$\text{Power lost in tube} = E_p \times I_p = OD \times CD$$

and the total power supplied by the battery must be the sum of these powers, that is

$$\text{Power from battery} = E_B \times I_p = OE \times CD$$

Now the area of the rectangle $CDEF = DE \times CD =$ power in load, and the area of the rectangle $ODCG = OD \times CD =$ power lost in tube, and the area of the rectangle $OEFG = OE \times CD =$ total power from battery.

When an a.-c. input is applied to the tube so that the grid is operated about its mean or average value of − 20 volts, the maximum a.-c. current through the load is given by the line HC and the maximum a.-c. voltage across the load is given by the line HB. Let us call these values of current and voltage

$$e_R = \text{maximum a.-c. voltage across load} = HB$$
$$i_p = \text{maximum a.-c. current through load} = HC$$

Since a.-c. power in a resistance circuit is the product of the r.m.s. current and the voltage, to obtain the a.-c. power in the load we must first get the r.m.s. values of the above values and then multiply them

$$e_R \text{ r.m.s.} = e_R \text{ max.} \times \frac{1}{\sqrt{2}}$$

$$i_p \text{ r.m.s.} = i_p \text{ max.} \times \frac{1}{\sqrt{2}}$$

whence a.-c. power in load $= e_R\, i_p$ (r.m.s.)

$$= e_R \times i_p \times \frac{1}{\sqrt{2}} \times \frac{1}{\sqrt{2}}$$

$$= \frac{e_R \times i_p}{2}$$

$$= \frac{HB \times HC}{2} = \text{area of triangle } HCB.$$

This power is dissipated in the load resistance in addition to the d.-c. power lost there due the voltage drop across it and the current through it. Since the average current drawn from the battery has not changed, the power taken from the battery has not changed—and yet the load has an additional amount of power used up in it. Where does this power come from? Clearly it must come from the power used up on the plate of the tube. *When an a.-c. voltage is placed on the grid, then a.-c. power is developed in the load, less power is wasted on the tube plate, and the tube will actually run cooler when it is delivering power to the load than when standing idle, that is, with no a.-c. input grid voltage.*

Let us see what these values of power are. We can take them directly from the graph in Fig. 148.

d.-c. power lost in load (no a.-c. grid voltage)

$= DE \times CD = (260 - 160) \times (20 \text{ ma.})$

$= 100 \times .02 = 2$ watts

d.-c. power lost in tube (no a.-c. grid voltage)

$= OD \times CD = (160) \times (20 \text{ ma.})$

$= 160 \times .02 = 3.2$ watts

d.-c. power taken from battery

$= OE \times CD = 260 \times .02 = 5.2$ watts

max. a.-c. voltage across a load (a.-c. grid voltage = 10)

$= HB = 210 - 160 = 50$ volts

max. a.-c. current through load (a.-c. grid voltage $\doteq$ 10)
$= HC = 10$ ma. $= .01$ ampere

a.-c. power in load (a.-c. grid voltage = 10)
$\frac{1}{2} \times HB \times HC = .5 \times 50 \times .01 = .25$ watt
= 250 milliwatts, which is subtracted from d.-c. power in tube.

In Section 180 the formula for the power output of a tube was stated to be

$$\text{power output} = \frac{\mu^2 e_g{}^2 R}{(R_p + R)^2}$$

and in order to check the above calculations we must find the tube constants from the curves in Fig. 148. The plate resistance of the tube is simply the reciprocal of the slope of the E_p–I_p line, and noting that a change of 160 – 100 volts on the $E_g = -10$ line produces a change in plate current of from 42 to 25 ma. we calculate

$$R_p = \frac{160 - 100}{.042 - .025} = \frac{60}{.017} = 3500 \text{ ohms},$$

and from the two curves, $E_g = -10$ and $E_g = -20$ we ascertain that a change of 10 volts on the grid produces a change in plate current of from 42 to 20 ma. when the plate voltage is 160, we calculate

$$G_m = \frac{.042 - .020}{10} = 2200 \text{ micromhos}$$

whence

$$\mu = R_p \times G_m = 3500 \times 2200 \times 10^{-6}$$
$$= 7.7$$

whence power output

$$= \frac{(7.7 \times 7.07)^2 \times 5000}{(5000 + 3500)^2}$$
$$= .206 \text{ watt} = 206 \text{ milliwatts.}$$

This value agrees closely enough with our data secured from the characteristic curves in Fig. 148.

Thus from a collection of the E_p–I_p curves of any tube we may obtain all the necessary data upon which to build an amplifier and calculate its power output, the losses in the various tubes, the percentage distortion, etc.

190. The pentode.—A triple-grid tube which has come into general use in Europe and which is coming to some prominence

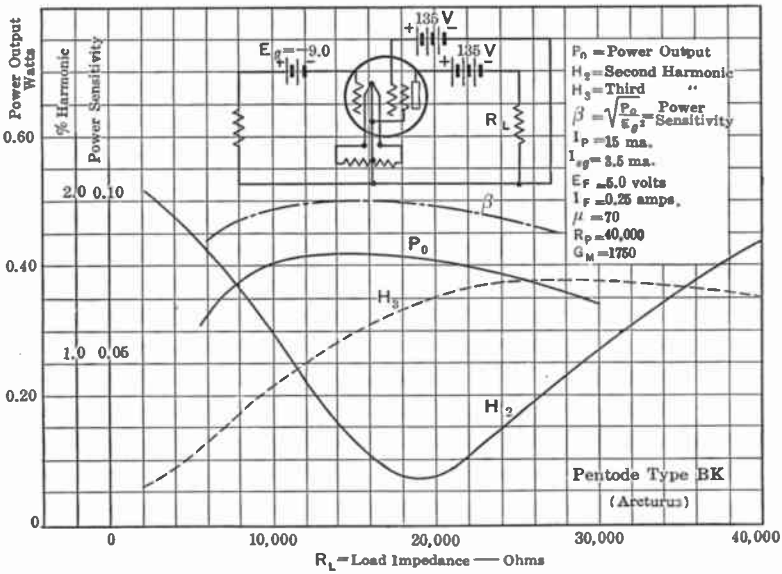


FIG. 149.—Power output and harmonic content of output of pentode tube.

in this country is the pentode, a power output tube. One grid is permanently attached, within the tube, to the filament, another is connected to the plate voltage, and the third is the signal grid. The cathode grid (attached to the filament) forms a wall through which electrons emitted from the plate due to impact of normal electrons from filament, cannot break through to reach the other elements.

The advantage of the tube is its superior sensitivity compared to a three-element power tube. With comparatively small input voltages considerable power output can be secured. Its disadvantage is that considerable third harmonic distortion exists in its plate circuit. The tube is a high-mu, high plate resistance tube, and should work into a load resistance considerably less in value than the resistance of the tube.

Wherever a tube giving considerable output with small signal input is desired, e.g., automobile radios, police receivers, airplane sets, etc., the pentode fits in. It is a space-saving, amplification-saving tube. It is probable that many hundreds of them will find their way into radio receivers for special purposes and perhaps be generally used in home receivers when the technical problems connected with their use have been completely studied and solved.

The tube is specially valuable when detectors overload. Using a pentode instead of a three-element power tube, the detector need not put out as much voltage, and hence its input may have to handle smaller voltages.

Experiment 2–10. Remembering that the effective plate voltage may be calculated from

$$E = E_p + \mu E_g$$

and that E_g is negative use the data below to plot a family of E_p-I_p curves. A good way to do this is to fill in the table below with the essential data and then to plot it. After two or three curves are plotted, the others may be drawn without calculating the values of current because all curves are parallel. Calculate the mutual conductance, the amplification factor, the plate resistance. Calculate the slope of the load line (*AE* in Fig. 148); draw it in, and figuring 5 ma. as the minimum permissible value of plate current, calculate the maximum and minimum voltage across and current through the load, the power in it, the percentage distortion. Assume the efficiency is the ratio between a.-c. power in load and d.-c. power taken from the battery. Calculate the efficiency for several values of input a.-c. voltage.

E_p	$E_g = -0$	$E_g = -10$	$E_g = -20$	$E_g = -30$
150	20	10	......	......
200	30.2	18.5	......	......
250	42	29.0	......	......
300	54	......	......	......
350	66	......	......	......

I_p in ma.

Read

CHAPTER XI

AUDIO AMPLIFIERS

So FAR we have not spoken of the frequency or band of frequencies at which the vacuum tube and its associated apparatus will amplify. The theory up to the present point deals with amplifiers in general. It is necessary now to consider the types of amplifiers, and their differences.

191. Need of an audio amplifier.—Practically all radio receivers in use at the present time consist of three parts: a radio-frequency amplifier, a detector, and an audio amplifier. Because of the simplicity of audio amplifiers, and because of their greater application, we shall consider them first.

Let us think of the broadcasting studio in which originate the signals which we must amplify. A microphone stands in front of a musician or a speaker. It has two electrodes which for the sake of our discussion may be made of carbon. Between them is a little box of carbon granules. One of the electrodes has a metal diaphragm attached to it which is so located that the air vibrations we call sound impinge on it. When sound is directed into the microphone it moves the diaphragm which in turn moves one of the electrodes which squeezes the carbon granules and thereby changes their electrical resistance. The steady battery current which normally flows through the microphone from one carbon electrode through the carbon granules to the other electrode is changed in accordance to the frequencies of the music or speech directed into it.

This steady current of the microphone is said to be "modulated" or changed in accordance with the voice frequencies; and after the steady current is filtered out, the changes are built up in strength by amplifiers which will transmit the range of frequencies that will be encountered in practice. Here then is the first need for amplifiers. They must make up the loss resulting from transferring the energy in the moving air particles we call sound into the energy of the changing electric current. This loss in energy that must be made up is considerable.

The frequencies normally transmitted over telephone lines range from 250 to about 2500 cycles. These are complex audio-frequency a.-c. currents. Most of the energy of the voice occurs in the frequencies below 1000 cycles, most of the intelligibility above that frequency; therefore if a filter is put in the telephone line which admits only frequencies below 1000 cycles we would hear a sound but it would be unintelligible. On the other hand, if the filter cut out all the low tones and transmitted only those above 1000 cycles, we could understand what the speaker was saying, but the sound would not carry, it would be weak.

For best intelligibility and carrying power—naturalness, we say—all the frequencies from about 120 to 2500 are necessary for transmission of speech.

Music, however, is more complex and for realism and naturalness a much greater frequency range must be transmitted, not only by the microphone but also by the amplifiers, the radio broadcasting station, the ether, the radio-frequency amplifier or the receiver, and finally the audio amplifier and loud speaker in one's home. Music requires the transmission of all frequencies between 100 and 5000 cycles per second, and many critics—especially in Europe—desire that a still greater range shall be transmitted. At the present time, in the United States, the best broadcasting stations and connecting circuits transmit from slightly below 100 to about 5000 cycles per second. After a certain amount of amplification these tones are mixed with a radio-frequency wave which is emitted from the antenna of the transmitting station. Just as the microphone current is said to be modulated, so is the radio-frequency wave of the station said to be modulated by these amplified audio-frequency tones.

In spite of the fact that considerable power is used at the broadcasting station evidenced by the strength of the signals that leave the antenna, there is an enormous loss in signal strength as we go away from the transmitter. These radio-frequency waves modulated at audio frequencies are greatly reduced in strength owing to absorption and dissipation in the medium through which they travel. It is now our duty to make up the transmission losses, to amplify them again, to demodulate or separate the audio- and radio-frequency currents, and then to forget all about the radio circuit from then on.

An audio amplifier, then, has nothing to do with radio at all, and can be used to amplify any voice or music frequency-modulated electric currents that are placed upon its input. Its job is to build up the strength of a minute electric current to the point where the audio modulations on this current are of equal or greater strength than they were originally.

From the moment the sound in the studio enters the microphone, it ceases to exist as sound, and becomes an electric current. The steady or d.-c. microphone current, in such a system, is a carrier for voice or music-frequency modulations, just as the steady or average d.-c. plate current of a vacuum tube is a carrier for the a.-c. plate currents that flow there. So too is the radio-frequency a.-c. current flowing in the transmitting antenna. So too is the radio-frequency current flowing in one's receiving antenna and in the plate circuits of one's amplifiers. No sound is emitted again until some translating device is used, a device that will have electric currents in its input and sound or air waves in its output. Then, and only then, is sound emitted. Nowhere along the line from microphone to loud speaker can the signal be heard, unless some translating device is "plugged in."

The voice-frequency currents that can be amplified by an audio amplifier may come from a phonograph "pick-up," a telephone transmitter mouthpiece, or the plate circuit of a detector tube in a radio receiver. The radio link is, then, only an incidental and extremely inefficient part of the whole system—better results could be secured by eliminating the radio link completely and using telephone or power lines between the receiver and the transmitter. The advantage of radio is the ability to "broadcast" in all directions, and to eliminate the need of a metallic circuit between the person broadcasting and the person listening.

Let us forget all about the radio part of our receiver, temporarily, and consider only the audio-frequency amplifier.

192. The requirements of an audio amplifier.—An amplifier to accept, transmit, and amplify audio-frequency tones has several requirements which have taxed the ingenuity of many engineers:

(1) The amplifier must transmit all the tones required, in their proper proportion. It must have no frequency distortion.

(2) The amplifier must amplify all frequencies properly whether the input voltage is high or low. It must have no volume distortion.

(3) It must have an overall amplification which added to the radio-frequency amplification will make up for the enormous loss of power between the input to the microphone and the output from the loud speaker.

Let us consider, for the moment, only the amount of amplification necessary. This value of overall amplification varies, of course, with the input signals possible, and the output power required. For home reception an output of one watt of electrical power into a loud speaker of average efficiency—perhaps 5 per cent—is sufficient, although many people get along with much less than this value, and some require much greater power outputs.

If the amplifier works out of the conventional "grid leak and condenser" detector tube, the maximum voltage available without distortion due to detector overloading is about 0.3 volt. If the loud speaker has a resistance of 4000 ohms and if we fix the output power at 0.7 watt there must be the following amplification:

W_o = power into load = 700 milliwatts

R_o = resistance of load = 4000 ohms

E_L = voltage across load E_o $= \sqrt{W_o \times R_o} = 53$ volts r.m.s.

E = total a.-c. voltage in plate circuit of last tube $= 53 \times 3/2 = 79$ volts

E_i = input voltage to amplifier = 0.3 volt r.m.s.

G = voltage amplification $= 79/0.3 = 260$ times

It is better that the amplifier shall have considerably more gain than this figure so that the detector may be worked at a safe distance below its overloading point—to have a good factor of safety —and that weak signals from distant stations can " load up " the amplifier and its speaker.

In some modern receivers certain modifications have been made so that the detector output is sufficiently high that a loud speaker can be operated on but one stage of audio amplification. (See Section 281.)

Let us say, then, that the minimum gain for our amplifier is 300 times. How can we secure this amplification? There are several ways and we have already discussed the various types of amplifier arrangements. It is only necessary so to design each stage or to add a sufficient number of stages that the overall voltage amplification will be sufficient. The next problem is to see if the required frequency characteristic can be secured to prevent distortion due to over emphasis or discrimination at some frequencies.

Example 1–11. An amplifier has a voltage gain, up to the grid of the last tube, of 200. The last tube has a μ of 8 and a plate resistance of 5000 ohms. It works into an impedance of 10,000 ohms. The input to the amplifier is 0.1 volt r.m.s. Calculate the power into the resistance, the voltage across it and the ratio between this voltage and the input voltage to get the overall voltage amplification.

The a.-c. voltage on grid of last tube $= E_i \times G = 0.1 \times 200 = 20$ volts.

The a.-c. voltage in plate circuit of last tube $= 20 \times 8 = 160$ volts.

The a.-c. voltage across 10,000-ohm load $= 2/3 \times 160 = 106$ volts.

Power into load $= E^2/R = 106^2/10{,}000 = 1.2$ watts.

Voltage amplification $= E_o/E_i = 106/0.1 = 1060$ times.

Problem 1–11. What voltage gain must an amplifier have to deliver 1.5 watts to a 4000-ohm load in the plate circuit of a tube whose plate resistance is 2000 ohms if the input voltage to the amplifier is 0.3 volt r.m.s.?

Problem 2–11. The load of an amplifier is a 2000-ohm resistor. The plate resistance of the last tube is 2000 ohms and its μ is 3. The gain in voltage up to the grid of this last tube is 100. What input voltage is required to deliver 50 milliwatts of power?

Problem 3–11. Prove that if the load resistance is double the tube resistance, the voltage across the load is two-thirds of the total a.-c. voltage in the plate circuit of the tube and the voltage amplification is equal to the amplifica- up to the grid of the tube times the μ of the tube times 2/3.

Problem 4–11. If the load resistance is twice the tube resistance and the a.-c. voltage across the load is 100 volts, what must be the total a.-c. voltage in the plate circuit? If the μ of the tube is 8, what must be the grid a.-c.

voltage? If this is the r.m.s. voltage, what must be the minimum C bias of the tube to keep its grid from going positive?

Problem 5–11. The voltage gain per stage is 8. How many stages will be needed to produce an overall gain of 500? Remember that voltage gains are multiplied, not added. Estimate the gain as the total a.-c. voltage in the plate circuit of the last tube divided by the input voltage.

Problem 6–11. The voltage gain per stage is 10. What is the total voltage gain (total a.-c. plate voltage divided by input voltage) in three stages?

193. Cascade amplifiers.—It is usually necessary to use more than one stage of amplification, whether this is at high (radio) frequencies or at low (audio) frequencies. That is, an a.-c. voltage is applied to the grid of one tube and amplified; this amplified a.-c. voltage is used to drive the grid of another tube where it is again amplified. This voltage may again be amplified or used to drive the grid of a power tube whose function is not voltage amplification but the delivery of power from the B battery to a loud speaker. The first tube in a two-stage amplifier is designed to amplify the voltage alone, and the transfer of power either at maximum efficiency or at maximum output is not a consideration. The second tube, or the third in a three-stage amplifier, is designed solely for the purpose of delivering power to the load, whether this is a loud speaker, or group of speakers, or a telephone line where it may be again amplified and put into the loud speakers. When two or more amplifiers are connected " in series " they are said to be connected in " cascade."

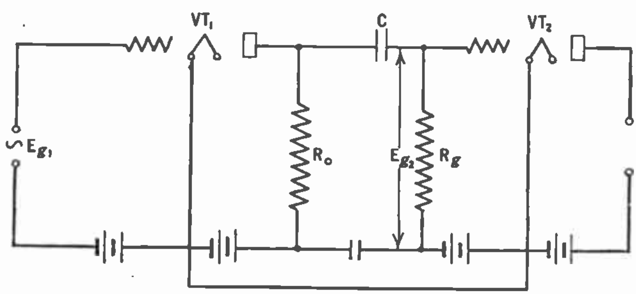


Fig. 150.—Two tubes coupled by a resistance-capacity unit.

194. Frequency characteristic of resistance amplifier.—Let us look at the circuit in Fig. 150 which gives two tubes coupled by means of a resistance-capacity unit. Voltage is fed to the grid of the first tube VT_1, is amplified there, and reappears across R_o. This amplified voltage is applied to the grid of the second tube and amplified, whence it reappears across whatever load is in its plate circuit. The voltage gain of such a stage is the ratio between the voltage on the second grid and the voltage on the first grid. That is,

$$G = \frac{E_{g_2}}{E_{g_1}} \tag{1}$$

We have already spoken about the conditions that result in maximum amplification in such a system, that is, the impedance in the plate circuit of the first tube must be large compared with the plate resistance of that tube. That is, the equivalent impedance of R_o shunted by C and R_g in series must be large compared to R_p (Fig. 151).

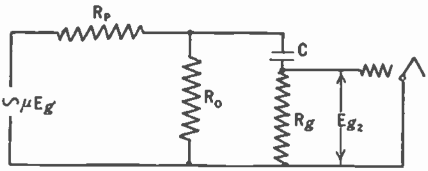


FIG. 151.—Equivalent circuit of Fig. 150.

Now the only part of this circuit which has a different impedance at different frequencies is the condenser. To get a good frequency characteristic, then, it is necessary to choose a value of C which will transmit the lowest frequency desired, because all other frequencies above this limit will find less impedance than this value. (The reactance of a condenser decreases with increase in frequency.) It is necessary to define the loss which we will tolerate in this condenser.

The voltage that is developed in the plate circuit of VT_1 is divided between the plate resistance of that tube and the load in the plate circuit. The voltage across this impedance is the output voltage, and is divided between that lost on the condenser reactance C and the grid resistance R_g of the following tube. The only useful part is that appearing across R_g. The ratio between the voltage across R_g and the voltage across the grid of tube 1 is

$$\frac{E_{g_2}}{E_{g1}} = \frac{\mu R_g R_o}{(R_p + R_o)\sqrt{R_g^2 + X_c^2} + R_o R_p} \tag{2}$$

where R_p, R_o and R_g are in ohms and C is in microfarads.

This ratio represents the efficiency of the whole system from the grid of tube 1 to the grid of tube 2. Now if the equivalent resistance in the plate circuit of tube 1 is called R'_o and if the tube's internal plate resistance is R_p, the amplification possible is

$$\mu \times \frac{R'_o}{R_p + R'_o} \tag{3}$$

and the efficiency of transmission will be

$$\frac{R'_o}{R_p + R'_o} \tag{4}$$

and as described in Section 179 if $R'_o = 3\ R_p$ the voltage amplification will be 75 per cent of μ of the tube; that is,

$$\mu \times \frac{3}{3+1} = \mu \times \frac{3}{4} = \mu \times .75.$$

All of this output voltage, however, is not impressed on the grid of the next tube. Some of it is lost in the reactance of the condenser. The voltage across the coupling resistance R_o, then, is divided between the reactance of the condenser and the resistance of the grid lead, R_g.

Let us assume that the voltage across the coupling resistance is constant, and see what the relation between the value of C and the grid leak resistance must be for maximum amplification and best frequency characteristic.

This a.-c. voltage across the condenser and the grid leak in series will produce a current

$$i = \frac{E_{Ro}}{\sqrt{R_g^2 + X_c^2}} \tag{5}$$

and the voltage across the grid leak—which is the useful voltage—will be

$$E_{g_2} = iR_g \tag{6}$$

Now let us call N, the ratio between E_{g_2} and E_{R_0}, the percentage of amplification of the full voltage, E_{R_0}, which we want to secure across the grid leak.

$$N = \frac{E_{g_2}}{E_{R_0}} = \frac{R_g}{\sqrt{R_g^2 + X_c^2}} \tag{7}$$

from which we can get the value of C.

$$C = \frac{N}{2\,\pi f\,R_g\,\sqrt{1 - N^2}} \tag{8}$$

which states that the condenser C must have the value given in formula 8 if we are to get N per cent of the voltage E_R actually and usefully impressed across R_g.

Now we can see at once that the proper value of C depends upon two factors: first the frequency and second the resistance of the grid leak. And so we find that not only does the voltage usefully impressed depend upon C and R_g, but that the frequency characteristic, as well, depends upon these factors. It is not difficult to see that the frequency characteristic should depend upon a condenser, C, but the fact that it also depends upon a resistance—which in itself has no frequency characteristic—is often overlooked. For every value of C there is a certain value of R_g which will permit maximum amplification at a definite frequency. The amplification will be greater than this value at all frequencies above this figure.

The relation between these factors is shown in the table below.

N = 90 per cent at 50 cycles		N = 80 per cent at 50 cycles		N = 70 per cent at 50 cycles	
C, mfd.	R_g, meg.	C, mfd.	R_g, meg.	C, mfd.	R_g, meg.
0.0132	0.5	0.0084	0.5	0.0062	0.5
0.0066	1.0	0.0042	1.0	0.0031	1.0
0.0033	2.0	0.0021	2.0	0.00156	2.0
0.0013	5.0	0.0008	5.0	0.0006	5.0

Calculation will show that when $N = 80$ per cent at 50 cycles $N = 93$ per cent at 100 cycles, and for all values over 100 cycles N is almost unity—that is, nearly all of the available voltage is usefully employed. An interesting relation may be secured from this formula for C. It is

$$CR_g = \frac{N}{\omega\sqrt{1 - N^2}}, \tag{9}$$

and to attain $N = 90$ per cent at 50 cycles the capacity of C in microfarads times the resistance of R_g in megohms must be .006. That is, at 50 cycles a 0.006-mfd. condenser and a 1-meg. grid leak will give 90 per cent of the total voltage available across R to be usefully applied to the following tube. Now if one stage of resistance amplification gives 90 per cent of the possible amplification at a given frequency, two stages will give (90 per cent)^2 or 81 per cent of the possible amplification considering the ratio between the output of the second tube and the input to the first. If the overall amplification of the two stages is to be 90 per cent of the maximum possible, the value of N per stage must be the square root of 90 per cent or .95 approximately. The curves in Fig. 152 illustrate this effect. They were taken from the Proceedings of the Institute of Radio Engineers, December, 1926, "The Design of Resistance Capacity Coupled Amplifiers," by Sylvan Harris.

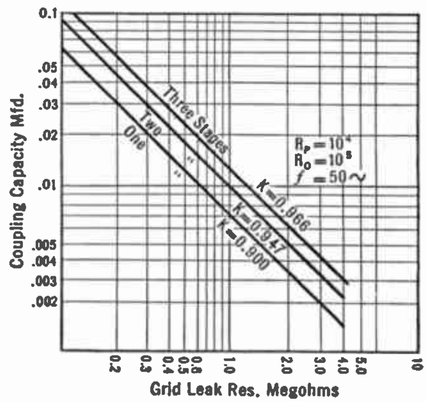


FIG. 152.—Relation between grid leak resistance, coupling capacity and efficiency (K or N).

If, then, we choose the value of R, R_g, and C properly we can attain any desired percentage of the μ of the tube at any frequency. To transmit low frequencies properly requires a larger product of C

times R_g. The question remains, how much amplification can be attained?

Problem 7–11. Assume the following values and calculate the efficiency: $C = 1$ mfd.; $R_g = 500{,}000$ ohms, $R_o = 200{,}000$ ohms, $R_p = 60{,}000$ ohms, $f = 800$ cycles, and $f = 40$ cycles.

Problem 8–11. The μ of a tube is 30 and its plate resistance is 60,000 ohms. Calculate and plot the voltage amplification as the load resistance varies from 10,000 ohms to 200,000 ohms.

Problem 9–11. A condenser and a grid leak are in series. $C = 0.006$ mfd., and $R_g = 2$ megohms. Across them is a 40 cycle-voltage of 10 volts. Calculate the current flowing, the voltage drop across C and across R_g; and, assuming the voltage across R_g is the only useful voltage, calculate the efficiency by dividing the voltage across R_g by the total voltage and multiplying by 100 per cent.

Problem 10–11. A frequency of 100 cycles is to be transmitted across the grid leak and condenser in Fig. 150 at 90 per cent efficiency. If, then, $N = 0.9$, $R_g = 500{,}000$ ohms, what must C be in microfarads?

Problem 11–11. Calculate what the product of $C \times R_g$ must be for any given values of N. That is, solve for $C \times R_g$ in equation (8). Then assume various values of f from 100 to 10,000 cycles and plot products of $C \times R_g$ to give a constant value of N.

Problem 12–11. What is N if $C = 0.006$, $f = 20$ cycles, and $R_g = 1$ megohm?

195. Overall amplification.—Let us consider a three-stage amplifier, having resistances, tubes, etc., as shown in Fig. 153.

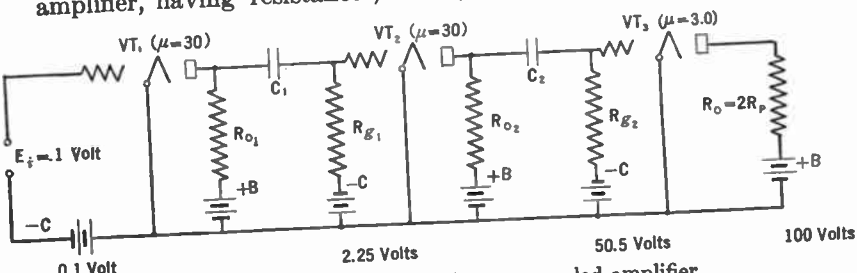


FIG. 153.—Three stage resistance coupled amplifier.

The first two tubes have an amplification factor of 30, the final or power tube has a μ of 3. What is the overall voltage amplification? If the values of R, C, and R_g are properly chosen, the amplification per stage will be 75 per cent of the μ of the tube, and what the first tube amplifies will be amplified again by the second. That is, if an input of 0.1 volt is applied to the grid-filament input of the first tube a voltage of $0.1 \times .75 \times 30$ or 2.25 volts will be applied to the second, and a voltage of $2.25 \times 30 \times .75$ or 50.5 volts to the third input; and if the resistance into which this tube works has twice the value of the plate resistance of the tube, two-thirds of the total a.-c. plate voltage of the last tube will be applied to the load. That is, the load will have across it a voltage equal to $50 \times 3 \times \frac{2}{3}$ or 100 volts.

The overall voltage amplification in such a case will be $100 \div 0.1$ or 1000. This is equal numerically to the product of the voltage gain of the individual stages. Thus if each stage has a gain of N, two stages will have a gain of N^2, three stages a gain of N^3, etc. In this case it will be $(22.5)^2 \times 3 \times 2/3 = 1000$ (approximately).

196. Plate battery requirements.—One of the objections to the resistance amplifier is the excessive plate battery voltages that are necessary. The voltage on the plate of a tube in whose plate circuit is a high resistance is not the voltage of the battery but this voltage minus the voltage drop across the resistor in the plate circuit. We want the a.-c. voltage drop across this resistance to be high but the d.-c. voltage drop to be low. As an example suppose a tube has a plate resistance, R_p, of 60,000 ohms when the plate voltage (E_p) is 100 volts. To get 75 per cent of the μ of the tube as the overall amplification from grid input voltage to the voltage output across the resistor, we need a resistance in the plate circuit of 180,000 ohms. Suppose under these conditions the plate current is 1 ma. What plate battery voltage is necessary if 100 volts are required on the plate?

The plate voltage may be found from

$$E_p = E_b - I_pR_p$$
$$100 = E_b - 0.001 \times 180{,}000$$
$$E_b = 280 \text{ volts.}$$

Now the tube will amplify with fewer volts on the plate than this—as many manufacturers and experimenters have proved—but the difficulty lies in the following fact. The plate resistance of a tube is a function of the plate voltage. That is, at low plate voltages the plate resistance is high, which in turn necessitates a higher value of load resistance to get the 75 per cent of the μ of the tube, which means that the voltage drop will be high across this resistor and so on. A high plate battery is always needed.

To get 100 volts on the plate of this tube requires a plate battery of 280 volts. This is inefficiency, of course. What can be done about it?

197. Inductance load amplifier.—Suppose instead of the resistor in the plate circuit we substitute a low resistance inductance with a high value of reactance at the frequencies at which the amplifier is to work, for example a 100-henry choke coil with a d.-c. resistance of 1000 ohms. The circuit looks like Fig. 154. Now the d.-c. plate current encounters no appreciable opposition in the 1000-ohm resistance. In fact the voltage drop is 1 volt per milliampere of plate current. The a.-c. current, however, must flow through the high inductance and the resistance in series. Across this impedance ($\sqrt{R^2 + L^2\omega^2}$) will appear the amplified a.-c. voltage which may be used to drive another amplifier stage if desired.

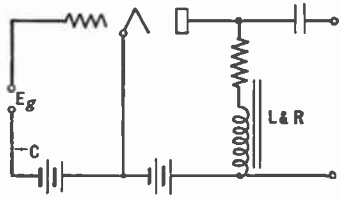


FIG. 154.—Inductance-capacity or "impedance" coupled amplifier.

Such an amplifier is commonly called an **impedance** amplifier. The loss in d.-c. voltage between the plate battery and the plate itself is only 1 volt per milliampere current, and if the plate current is 2 ma. only 102 volts of B battery will be required to put 100 volts on the plate of the tube.

Problem 13–11. An amplifier is to be used at audio frequencies. What must be the impedance of the choke coil at 100 cycles to secure an amplification of 7.5 from a tube whose μ is 10 and whose plate resistance is 15,000 ohms? What will be the amplification at 1000 cycles?

Problem 14–11. If the resistance of the choke coil used in Problem 13 is 500 ohms, what is the inductance required?

Problem 15–11. A tube has a load resistance of 100,000 ohms. The plate current is 2 ma. and the plate voltage required is 90 volts. What plate battery voltage is necessary?

Problem 16–11. A tube draws 0.5 ma. from the B batteries whose voltage is 180 volts. A coupling resistance of 100,000 ohms is used. What is the voltage actually on the plate?

198. Effect of stray capacities at high frequencies.—When one sets up a resistance amplifier in the laboratory and with a constant input voltage at various frequencies measures the voltage, the slight falling off at the lower frequencies is noted, but if the capacity of the coupling condenser and the grid leak are properly proportioned the droop at 100 cycles or below will not be pronounced. But the laboratorician will probably note a falling off at frequencies beyond 5000 cycles—which was not foretold by any of our mathematics or analysis up to the present moment. What is happening to the higher frequencies?

Let us look at Figs. 155 and 156 in which several additional capacities appear. These are made up of the internal plate-to-

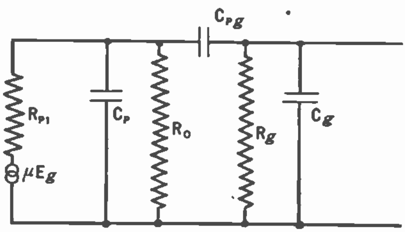


FIG. 155.—Equivalent circuit at high frequencies of resistance-capacity coupled tubes.

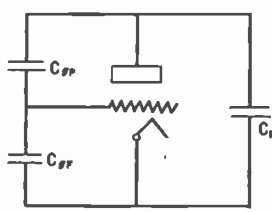


FIG. 156.—Tube capacities.

filament capacity of tube 1, the combined plate-to-filament and grid-to-filament capacity of the tube 2, and capacities in the sockets, wiring, etc. All of these capacities are directly across the grid-leak resistance or the input to the second tube. Their effect is small at low frequencies because they are small capacities, and have high reactances at low frequencies. They are, then, bridging impedances of very high value and consequently have little effect at low frequencies. But at high frequencies their impedance decreases, and by-passes some of the high-frequency voltages that normally appear across the grid leak. The higher the frequency, and the greater the effect of these additional and unavoidable capacities, the greater the droop of the curve representing the response of the amplifier plotted against frequency.

The droop at high frequencies depends too upon the overall gain of the amplifier; therefore when we boost the gain by using a large coupling resistance, R_o, we do get more amplification in the middle of the audio-frequency band, but a more decided drop at both low and higher frequencies.

These effects are illustrated in the curve in Fig. 157, taken from a Radio Club of America paper by A. V. Loughran, published in *Radio Broadcast*, August, 1927.

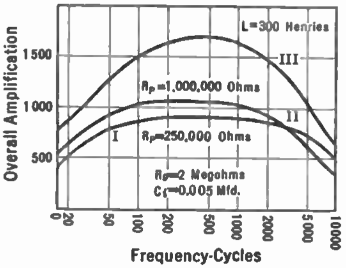


FIG. 157.—Frequency characteristic of resistance- and inductance-coupled amplifiers.

The small capacity existing between the filament and the grid, etc., is due to the fact that they are made up of conductors insulated from each other; our definition of a capacity. They are at different potentials. In addition there are capacities existing between the terminals on the tube socket, and in the wiring of the amplifier. All in all, these unwanted and undesirable capacities may ruin an otherwise perfect amplifier—and they must always be reckoned with.

Not only do these capacities, which are represented in Fig. 155, play havoc with high frequencies, but the effect of the grid-plate capacity of the second tube is multiplied by the μ of the tube—a very interesting and unfortunate fact.

The capacities which cause trouble at high frequencies are:

(1) Grid-filament capacity, C_{gf}.
(2) Plate-filament capacity, C_{pf}.
(3) Plate-grid capacity, C_{gp}.
(4) Stray capacities in wiring, etc.

The capacity C_g across the input to the tube is equal to

$$C_g = C_{g_f} + C_{g_p}\,(\mu_o + 1),$$

where μ_o is the effective amplification in the circuit, and the other factors are as itemized above and shown in Fig. 155.

These values for the Radiotron UX–240, a tube adapted for resistance-coupled amplifiers, are $C_{p_f} = 1.5$ mmfd., $C_{g_f} = 3$ to 4 mmfd., and $C_{g_p} = 8.8$ mmfd. In practice C_g may vary from 20 to as high as 300 mmfd. depending upon the intrinsic values of its components and the amplification of the system. That is, if the $C_{g_f} = 3.0$ mmfd., and $C_{g_p} = 8.0$ mmfd. and the effective amplification of the system is 20, C_g becomes 3 plus 8 × 20 or 163 mmfd. —which is an appreciable capacity and not at all what one would expect. The 201–A has about the same inter-electrode capacity and the UX–171 has somewhat greater grid-filament capacity owing to the longer electron-emitting surface. The effective capacity across the input to the tube is a function of the μ of the tube; thus the greater the amplification factor the more trouble one gets into because of this capacity-multiplying effect. Low μ tubes are not so troubled, but their amplification is low; and so the amplifier designer and experimenter must compromise between a good frequency characteristic and a high gain. If the gain is good the high frequencies are discriminated against, and if the characteristic is very good the overall gain is likely to be low.

Problem 17–11. The μ of a tube is 8, its grid-filament capacity is 6 mmfd., its plate-grid capacity is 8.0 mmfd. The effective amplification of the circuit is 7, and stray capacities across the filament and grid circuit amount to 2 mmfd. What is the effective shunting capacity C_g?

199. Quantitative effect of capacities on high frequencies.— How much do these shunting capacities cut down the high frequencies? The effective resistance of a resistance shunted by a condenser (as C_p and R_o in Fig. 155) is:

$$r = \frac{R}{1 + \omega^2 R^2 C^2},$$

and in the table below may be found some values of the effective resistance of a quarter-megohm resistor shunted by 60 mmfd. capacity.

Frequency	Effective resistance (ohms)
2,000	240,000
4,000	220,000
6,000	190,000
8,000	160,000
10,000	130,000

If the resistor is 1 megohm and if the shunting capacity is 300 mmfd., the effective resistance will be only 2800 ohms at 10,000 cycles although it is 960,000 ohms at 100 cycles—a drop of 97 per cent.

These figures show that the higher the plate-coupling resistance the greater will be the discrepancy between the amplification at 10,000 and 100 cycles. This is because the reactance of the capacity is the same at 10,000 cycles whether it is across 1 megohm or across $\frac{1}{10}$ megohm, but the shunting effect in the first case is much greater than in the second. Thus if 10,000 ohms is shunted across 1 megohm, the resultant decrease in impedance will be from one million ohms to not far from ten thousand ohms or a reduction of one hundred times. If, however, it is shunted across 100,000 ohms it has decreased the impedance only ten to one.

Example 2–11. Suppose a 1-megohm resistor is in the plate circuit of a tube and that 10 volts are developed across it. If 100,000 ohms are shunted across it, the effective impedance becomes 0.91×10^5, and if the current is the same the voltage developed has been reduced by 91 per cent. Now, suppose 10 volts are developed across 100,000 ohms and that another 100,000-ohm resistor is shunted across it. What is the resultant reduction in voltage? Clearly it is 50 per cent—a much smaller percentage reduction.

Problem 18–11. A tube with an amplification factor of 30 and a plate resistance of 150,000 ohms is used with a half-megohm coupling resistance. Suppose that in construction a path of soldering flux is placed across the terminals of this resistor accidentally so that the half-megohm is effectively shunted by 100,000 ohms. What is the resultant amplification? What is the amplification without the shunting resistance? What is the percentage loss due to the flux?

These capacities within the tube and those due to the socket and the wiring reduce the amplification at the higher audio frequencies and make impossible a flat characteristic with high overall gain. If one stage loses 50 per cent of the response at 5000 cycles, two of them will lose 75 per cent and three of them 87.5 per cent, and so on.

The curve in Fig. 157 showing the recommended values for use with the UX–240 tube is a very good characteristic, and equals many and betters some of the amplifier characteristics obtained by other coupling devices.

200. High-frequency response in impedance-coupled amplifiers.—The main disadvantage of the resistance amplifier, that is, large B battery voltages, may be overcome by using high inductance chokes instead of the resistor, but the loss at high frequencies is even worse because of the distributed capacity of the winding of the choke. A characteristic using 300-henry chokes appears in Fig. 157 and as may be seen is worse than the resistance-coupled stages. It is possible to design a better choke than was used in this experiment, but even then great care must be taken to preserve a good frequency characteristic.

201. Tuned inductance amplifier.—In both the resistance load and the inductance load amplifier the maximum amplification is attained when the impedance in the plate circuit is a maximum. If, then, we desire to transmit only one frequency, say 1000 cycles, we can get greater amplification by tuning the inductance with a shunt condenser so that we have an anti-resonant circuit in the plate circuit of the tube, as shown in Fig. 158. If an inductance of 0.1 henry is tuned with a 0.254-mfd. condenser the resonant frequency will be about 1000 cycles. If the coil has a resistance of 100 ohms the impedance of the anti-resonant circuit will be roughly 3950 ohms whereas the reactance of the coil alone will be only 628 ohms. Tuning the coil therefore increases the load impedance in the plate circuit by about 6.3 times.

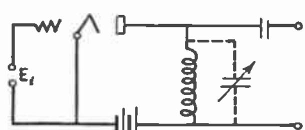


FIG. 158.—Tuned inductance output.

The voltage gain will be given by the formula of Section 178:

$$G = \mu \frac{R_o}{R_o + R_p},$$

which shows that the maximum possible amplification is the μ of the tube, and, as we have already seen, increasing the load impedance R_o to the point where it is three times the tube internal resistance results in a voltage amplification of $\mu \times .75$.

Problem 19-11. An inductance of 170 microhenries has a resistance of 6.0 ohms at 500 kc., 10 ohms at 1000 kc., and 18 ohms at 1500 kc. Assuming a fixed capacity—due to distributed capacity of winding, connections, etc.—across the coil of 60 mmfd., calculate the condenser capacity that will tune the coil over the broadcast frequency band. Calculate the reactance of the coil at the three frequencies above and the voltage gain to be expected when used with a tube whose plate resistance is 12,000 ohms and a μ of 8. Then calculate the impedance in the plate circuit if the inductance is tuned at each of the three frequencies and the voltage gain to be expected when connected as in Fig. 158. Plot the voltage amplification of this single stage against frequency. Explain why the curve is not flat.

The untuned inductance or "impedance" amplifier can be used where it is desired to transmit a fairly wide band of frequencies; tuning it makes it possible to get greater amplification over a narrow band of frequencies.

202. The transformer-coupled amplifier.—The output a.-c. voltage across the resistance or inductance—tuned or not—can never be higher than the input grid voltage multiplied by the μ of the tube, and can attain that value only when the resistance or impedance is high compared to the plate resistance. Suppose, however, we use a transformer, as in Fig. 159. The voltage across the secondary will be increased by the turns ratio of the windings and so the voltage developed in the plate circuit of the tube may not only be passed on to a following tube multiplied by the μ of this tube but multiplied by the turns ratio as well.

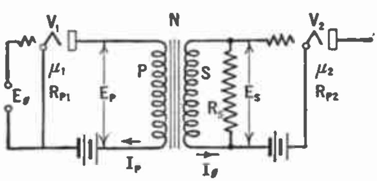


FIG. 159.—Transformer coupled amplifier

If the secondary circuit takes no current or power the greatest voltage will appear across the secondary when a very high turns ratio is used, but this is not the case when power is taken—and some always is.

The maximum voltage across the secondary will be obtained when the turns ratio is given by the expression

$$N^2 = \frac{R_s}{R_p},$$

where R_s and R_p are the resistances between which the transformer works. When such a turns ratio is used the voltage across the secondary is given by

$$E_s\,(\text{max.}) = \frac{\mu_1\, E_{g_1} N}{2}. \qquad (7)$$

All of this assumes that a perfect transformer is used, that is, one which has no d.-c. resistance, no magnetic leakage, and infinite primary and secondary reactances. If the resistance of the load across the secondary is 1 megohm, and the plate resistance of the tube is 10,000 ohms, the proper turns ratio,

$$N = \sqrt{\frac{1{,}000{,}000}{10{,}000}} = 10,$$

and the voltage gain from (7) is

$$\frac{E_s}{E_{g_1}} = \mu_1 \times 5 = 40 \text{ if } \mu_1 = 8.$$

The foregoing mathematics discloses several interesting points. In the first place it is possible to get much greater voltage amplification by means of a transformer than is possible with the same tube and either resistance or inductance output. In the second place, for every ratio of resistance across the secondary and primary of the transformer there is a certain turns ratio which will produce the maximum voltage step-up. This means that once the resistances on either side of the transformer are determined, the turns ratio for maximum voltage gain is fixed. This, in turn, means that a transformer can be used as an impedance adjusting device, that is, a coupling device between two circuits of different impedance, one of which acts as a source of voltage and the other is the recipient of a voltage, amplified or not.

Whenever the impedances of the two sides of the transformer are not that indicated by the expression above, there is a loss in secondary voltage, a transmission loss, engineers say. Whenever two circuits are to be coupled together with the least loss in voltage or power the proper turns ratio transformer must be used, that is, $N^2 = Z_s/Z_p$, where Z_p and Z_s are the impedances between which the transformer works.

Problem 20–11. A tube whose plate resistance is 12,000 ohms (UX–201–A) works into a resistance, R_o, of 600,000 ohms. What is the proper turns ratio, and what is voltage gain if $\mu = 8$? If $E_{g_1} = 1$ volt what voltage will appear across R_o?

Problem 21–11. One tube whose plate resistance is 25,000 ohms is connected to another whose grid circuit has a resistance of 400,000 ohms. What is the turns ratio of the transformer for maximum voltage amplification?

Problem 22–11. An "output" transformer is to be used to connect a loud speaker to a tube. The impedance of the loud speaker at the desired frequency is 4000 ohms, the tube has a resistance of 2000 ohms. What is the proper value of N?

Problem 23–11. A telephone line has an impedance of 600 ohms. The a.-c. voltages in the plate circuit of a 6000-ohm tube are to be transferred to this line. What must be done to effect such a transfer with least power loss?

203. Transformer with no secondary load.—If the secondary of the transformer works into a true no-load impedance, that is, an open circuit, or R_g = infinity, the voltage appearing across the secondary will be μE_g multiplied by the turns ratio of the transformer and not, as given in (7) $\mu E_g \times N/2$. The voltage gain is equal to

$$G = \mu \frac{2\,\pi f L_1 N}{\sqrt{R_p^2 + (2\,\pi f L_1)^2}} = \frac{N\mu}{\sqrt{1 + \left(\frac{R_p}{X_L}\right)^2}}$$

where L_1 = inductance of the primary, etc.

Example 3–11. Transformers of a few years ago had very little primary inductance. Assume an inductance of 2 henrys, $f = 800$ cycles, $\mu = 8$, and

R_p = 10,000 ohms, $N = 4$. Calculate the voltage amplification. Then assume f = 80 cycles and calculate G.

$$G = 8\frac{2 \times 3.14 \times 800 \times 2 \times 4}{\sqrt{10^8 + (2 \times 3.14 \times 800 \times 2)^2}} = 22.7$$

If f = 80 cycles

$$G = 8\frac{2 \times 3.14 \times 80 \times 2 \times 4}{\sqrt{10^8 + (2 \times 3.14 \times 80 \times 2)^2}} = 3.2.$$

Problem 24–11. Assume a primary inductance of 50 henrys and calculate the gain per stage G using the other values used in Example 3. Assume f = 80, 800, and 8000 cycles and plot the characteristic, that is, gain against frequency.

204. The advantage of the transformer.—The tranformer has the great advantage that it can contribute toward the voltage amplification, and can contribute toward the maximum power output when the load resistance or impedance differs from the tube resistance. In addition, high B battery voltages are not necessary.

A transformer can be constructed so that it has little loss in itself. This loss is due the d.-c. resistance of the windings, the fact that perfect coupling between primary and secondary is not attained, and because of iron losses, that is, currents set up in the iron core represent a loss in power which must be supplied from the source. This power therefore does not get out of the transformer and cannot appear in the output.

If a good transformer is used, its transmission loss is small. Its effect, then, upon the circuit is of two sorts; first it may contribute toward the voltage gain by having a voltage step up in it; second, it may be used to "match" the load resistance to the tube resistance. Let us suppose the tube resistance is 10,000 ohms, and that the secondary load resistance is 100,000 ohms. A resistance of this value interposed in the plate circuit of a tube will not have the maximum power developed in it. (See Section 180.) But if we use the proper transformer such that $N^2 = 10$, this 100,000 ohms will look, to the tube, like a resistance of 100,000 × .01 or 10,000 ohms—the condition for maximum voltage and maximum power.

The transformer can always be forgotten if we substitute for it and its secondary load this load divided by N^2. Looked at from the secondary we may replace the transformer by $N^2 \times Z_p$.

Example 4-11. A transformer with a turns ratio of 3 connects a 10,000-ohm tube with a load which has a frequency characteristic such that at 100 cycles the load has one-tenth of the impedance it has at 1000 cycles. The load impedance at 100 cycles is 90,000 ohms. The μ of the tube is 8. What are the voltage amplification and the power output at 100 and 1000 cycles?

The transformer may be dispensed with in the calculation if we transfer the secondary load directly into the plate circuit of the tube by multiplying it by $1/N^2$, that is, 1/9.

Thus at 100 cycles the impedance in the plate circuit is

$$90{,}000 \times \tfrac{1}{9} = 10{,}000 \text{ ohms}$$

and the voltage amplification is

$$\frac{\mu \times R_o}{R_o + R_p} = \frac{8 \times 10{,}000}{20{,}000} = 4$$

and the power

$$P_o = \frac{\mu^2 E_g{}^2 R_o}{(R_o + R_p)^2}$$

$$= E_g{}^2 \times 1600 \times 10^{-6}$$

at 1000 cycles, $R_o = 900{,}000 \times \frac{1}{9} = 100{,}000$ ohms

and $G = \dfrac{8 \times 100{,}000}{110{,}000} = 7.3$ and $P_o = E_g{}^2 \times 533 \times 10^{-6}$

Problem 25-11. Assuming no loss in the transformer, what is the power transmitted to a 6000-ohm load from a 2000-ohm tube when they are coupled by a transformer whose secondary winding has 2.24 times as many turns as the primary? Assume $\mu = 3$, $E_g = 10$ volts r.m.s. Use formula (5) in Section 180. What would be the value of N for maximum power in the load? What would be the power then? What value of N would deliver maximum undistorted power output into the load? What is this value of power in milliwatts?

205. Effect of leaky condenser in resistance-coupled amplifier.—The coupling condenser C (Fig. 150) must have a very high d.-c. resistance, the resistors R_o and R_g must be quiet even though appreciable current goes through R_o and high a.-c. voltages appear across R_g. Suppose the preceding tube has a d.-c. plate resistance,

R_p, of 20,000 ohms under the conditions of operation, that is, 90 volts B battery, a coupling resistor of 60,000 ohms, and a plate current of 1 milliampere. Suppose the condenser has a d.-c. resistance of 10 megohms (10 million ohms) and that the grid leak of the following tube is 1 megohm. What happens?

Across the 60,000-ohm resistor is a 60-volt d.-c. voltage drop. This is impressed upon the two impedances, C and R_g in series, 11 megohms. By Ohm's law the current that will flow in this circuit is 5.45 microamperes, which across the 1-megohm grid leak produces a d.-c. voltage of 5.45 volts. This voltage is of such a polarity that the grid end of the grid leak is positive 5.45 volts. Suppose that the C bias is 4.5 volts and that a maximum or peak input voltage on the grid of this tube of 4.0 volts is expected. The actual C bias is 5.45 − 4.5 or 0.95 volts and so the tube is in imminent danger of going positive at any instant.

Let us suppose that the grid goes positive on a strong signal. It draws electrons from the stream leaving the filament and going toward the plate. These electrons make the grid negative, and if a sufficient number of electrons is trapped on it by a large positive overload the grid is so negative that the plate current is reduced to a very low value or even zero.

The tube now begins to "block," that is, the electrons may leak off to the filament at an audible rate and the tube emits "putt-putting" sounds which entirely destroy reception.

The grid of a resistance-coupled amplifier must never be allowed to become strongly positive, either by the introduction of too strong signals or through an improper C bias due to leakage of the B battery current voltage through the coupling resistor. If the grid is insufficiently biased and takes a momentary supply of electrons, these flow back to the filament through the grid leak and form a negative bias across this resistance. This bias aids the steady bias from the C battery and thus in a way tube overloading is self-correcting.

The condenser and grid leak are used in the inductance-coupled amplifier. If the resistance grid leak is replaced by a high-reactance, low-resistance choke, "blocking" does not occur so readily because the electrons leak off more rapidly.

206. Reflex amplifiers.—When two sets of frequencies of widely different order are to be amplified it is possible to make one tube serve as both a low-frequency and as a high-frequency amplifier. Such systems in which the energy from a tube is fed back into the input of a previous tube in a cascade amplifier is called a **reflex** system; although such systems are not in vogue at the present time they were of very great importance and interest in the early days of broadcasting. Let us look at Fig. 160.

Radio-frequency signals are impressed across the coupling coil

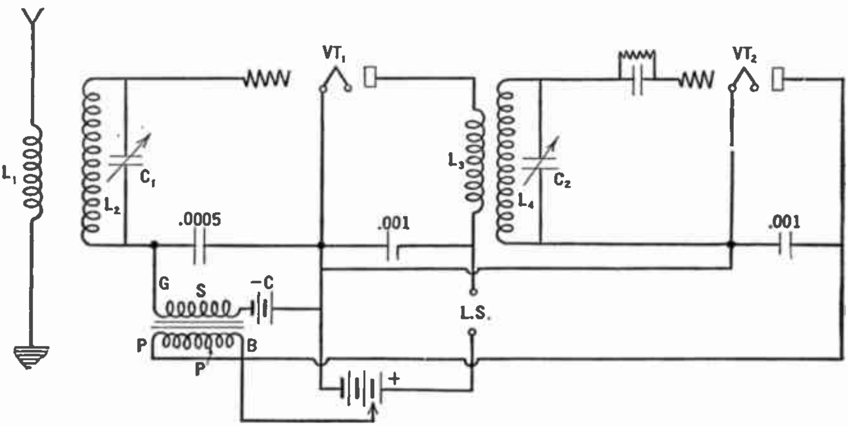


FIG. 160.—A reflex circuit. VT_1 amplifies both at low and high frequencies.

L_1 and from thence are transferred to L_2 where the required signals are selected by the tuned circuit L_2C_1. These voltages are amplified in the tube VT_1 and after a further selection process goes on in the tuned input, L_4C_2, are passed on to the tube VT_2 which is a detector. In the plate circuit of this detector tube the audio frequencies appear. They are passed back into the audio transformer secondary, S, which is in series with the grid of the VT_1. There is no voltage loss at audio frequencies in L_2 because it has practically no impedance at these frequencies compared to the impedance of the grid-filament path of the tube or of the transformer. In this tube the audio frequencies are amplified and are passed into the head phones or loud speaker or other audio amplifiers as noted at *L.S.* This load is by-passed by a large condenser so that no radio-frequency voltages are lost there. Of course there are audio-frequency voltages across the primary, L_3, of the inter-tube transformer but they are very small because this primary has practically no impedance to audio frequencies. And because of the very poor coupling to tube 2 at audio frequencies, practically no audio voltages appear across the input to the demodulator tube VT_2. We have then two tubes serving as radio-frequency amplifier, detector and low-frequency amplifier.

207. The inverse duplex.—The first tube in a radio set is the one which has the least work to do—the incoming signals are at their lowest level. The grid voltages are lowest in this tube. The next tube has greater signals to handle, and the final tube in a receiver must handle the greatest grid voltage swings. In the Grimes **inverse duplex** system, the first tube handles not only the low radio-frequency signal voltages but the strongest audio-frequency voltages, the second handles moderate radio-frequency and moderate audio-frequency voltages—and so no tube is overloaded with its double duty.

So long as the different sets of frequencies are far enough apart, the reflex amplifier works fairly well, but the difficulties of filtering together with poorer stability in such amplifiers militate against their wide use. In addition, tubes are not so expensive now but that the average experimenter prefers stability to a slight and questionable economy.

208. Transformer-coupled amplifiers.—The single transformer has already been discussed. It was stated in Section 202 that the maximum ratio for a transformer working between a 10,000-ohm tube and the input of another tube which might have an impedance of 1 megohm was 10 to 1. Unfortunately, this is only theoretically true, just as the calculations on resistance coupling without regard to certain factors produce erroneous results. A transformer to give a good low-frequency response when worked out of a detector tube—which normally has a rather high plate resistance—must have a primary inductance of about 100 henrys. Now a 9 to 1 transformer would have a secondary inductance of $9 \times 9 \times 100$ or 8100 henrys, and unfortunately such a transformer cannot be wound without its secondary having considerable capacity between layers of wire and between individual turns. This secondary distributed capacity shunts out the high frequencies just as the stray capacities in a resistance- or inductance-coupled amplifier lose the high audio tones.

It has not been found possible to build a transformer which will yield a flat frequency characteristic when worked out of a high impedance tube, and when using ordinary iron for the transformer core, with a turns ratio of much greater than 3 to 1. Using higher permeability iron, a somewhat greater turns ratio can be secured because less wire need be used to get a given value of inductance but there are very few transformers on the open market with a turns ratio of more than 4 to 1 that give a flat characteristic.

This statement does not preclude the possibility of using a higher ratio and overcoming the loss of either low or high tones—or both—in some other part of the circuit, and in fact many amplifiers have been so designed.

Figure 161 is a characteristic of a single transformer obtained by putting known voltages across the primary and measuring the secondary output voltage.

The hump at 5000 cycles is due the leakage inductance between primary and secondary resonating with the secondary distributed capacity. Beyond this point the whole transformer looks like a capacity to the tube and hence the effective resistance into which the tube works becomes steadily less as the frequency increases.

209. Measurements on transformer-coupled amplifiers.—The curve in Fig. 161 on a single transformer may be no indication at all of what a two-stage amplifier may do. This is due to the fact that a certain amount of "regeneration" takes place in the average amplifier unless considerable pains are taken to prevent such difficulties. This regeneration distorts the curve, and makes laboratory measurements impossible to check. One day the curve may be one thing, and on the next it may be different.

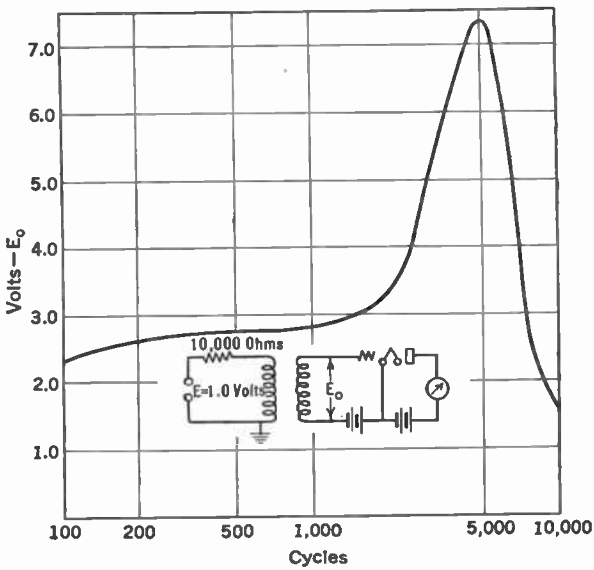


FIG. 161.—Characteristic of single andio transformer.

210. Calculation of overall voltage amplification.—Let us consider the amplifier in Fig. 162. The overall amplification is the

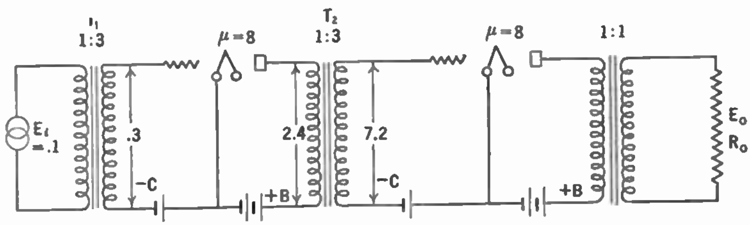


FIG. 162.—How a voltage E_i is amplified in a transformer coupled amplifier.

ratio between the voltage, E_o across the output load and that across the input, E_i.

$$G = \frac{E_o}{E_i} = \frac{3 \times 8 \times 3 \times 8}{E_i} \times \frac{R_o}{R_o + R_p}$$

$$= \frac{216\ R_o}{E_i\ (R_o + R_p)}$$

where R_p = plate resistance of last tube.

It is actually not possible to realize all this amplification because it is never possible to realize the full μ of the tubes. The voltage gain measured and calculated will check very closely, usually.

Now suppose we apply an input voltage of, say, 0.1 volt across the primary of the first transformer. Across the secondary this will become 3×0.1 or 0.3 volt and so the value of the C bias for this first tube which is fed out of the secondary of T_1 need not be greater than 1 volt since that will take care of severe overload, and if the tube is a 201–A type a plate voltage of 45 will be sufficient. Somewhat better amplification and fidelity will result by using 90 volts on the plate and 4.5 volts bias on the grid, since the plate resistance will be somewhat less under these conditions. If the impedance of the following transformer as looked at from the tube is high compared to the R_p of this first tube—as it will be at frequencies of the order of 1000 cycles if the transformer is any good at all—nearly all of the μ of this tube will be realized. Across the primary of the second transformer, T_2, then will appear a voltage of 0.3×8 or 2.4 volts and across the secondary a voltage of 7.2 volts which will require C bias of 9 volts and about 135 volts on the plate. The tube should be a 112 type. This voltage will be multiplied by 8 times in this tube and will appear across the output load as 35 volts provided the load is twice the resistance of the last tube. This voltage across a 10,000-ohm load will produce 122 milliwatts of power.

Now let us consider the combination of resistance and transformer coupling as shown in Fig. 163. In the constructor's mind there exists some doubt as to whether he should use the transformer next to the input or next to the power tube. Starting with an input of 0.1 volt the a.-c. voltages at various points in the circuit are as indicated. The second tube which has a resistance input must have a *C* bias of more than 2.4 volts, which means that the plate voltage must be rather high. If, on the other hand, the two resistance stages precede the transformer-coupled stage the *C* bias on the two tubes need not be very high, the plate resistance will not be so great, the coupling resistor need not have such a high resistance, and the B battery voltage can be lower in value.

Other combinations of transformer-, resistance-capacity, etc., amplifiers may be and are used.

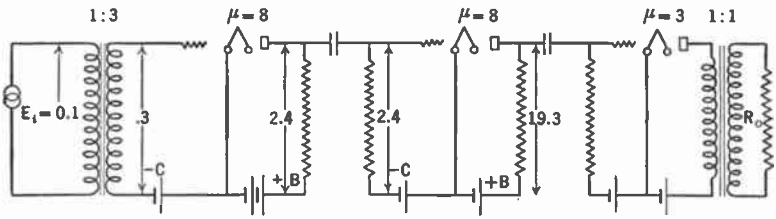


Fig. 163.—A combination transformer and resistance coupled amplifier.

211. "Equalizing."—It is possible by means of correcting circuits to get almost any kind of frequency response curve desired. For example, if a certain amplifier is deficient at low frequencies, one stage may be made resonant to these frequencies and so pull up the characteristic. If the amplifier tends to sing at some frequency, a loss may be put in at this frequency, and the overall curve will be flatter than without the equalizer. In the telephone plant the use of equalizing networks is very important and has come to be almost an exact science. These consist of resistances, inductances, and condensers. Equalizing usually results in an overall loss in amplification; that is, some loss is incurred which must be made up by additional stages. In other words one gains a better characteristic at the expense of amplification. In some amplifiers a better low-frequency response is secured by tuning the primary of the transformer by a capacity to a low frequency.

212. The power amplifier.—The final tube in an audio amplifier which is feeding audio frequencies into a loud speaker must be essentially a power amplifier. Its task is to deliver undistorted power to the loud speaker, and not to develop any great amount of voltage amplification. The task of the previous amplifier stages is to build up the small output voltages of the detector so that the large voltages necessary to swing the grid of the power tube may be obtained. The a.-c. power in the plate circuits of tubes previous to the power stage is small; what is required is that each previous stage shall give a maximum of voltage amplification without distortion, and the fact that maximum power may not be developed in these plate circuits is not important. These tubes work into very high impedances in which it is not possible to generate much power although it is possible to build up considerable voltages across them.

The a.-c. plate current of the last tube, then, must be rather large and this means that the grid a.-c. voltages must be large, which in turn means that the E_g–I_p curve of this tube must have a long and straight part. The 171 tube, for example, which can deliver about 700 milliwatts without much distortion must have an r.m.s. grid voltage applied to it of about 27 volts; there must be a portion of the E_g–I_p curve which is straight over at least twice this number of volts. Thus if the grid is biased 40.5 volts, the characteristic must be straight from minus 78.5 to minus 2.5 volts. The next preceding tube has much smaller voltage swings to handle and so its characteristic need not be straight over such a long part.

Because of the high cost of power apparatus when power tubes requiring high voltages are used, the final tube in the average radio receiver is a low μ, low-resistance tube which will deliver considerable power to the loud speaker without demanding excessive plate voltages. Such tubes require large input a.-c. voltages and therefore require greater amplification before them than tubes of higher values of μ. This can be looked at in another way. Modern receivers have considerable amplification, and, to prevent any danger of overloading power tubes with consequent distortion, it is necessary to use tubes with considerable C bias and capable of handling large swings of voltage. The power tube of the 171, 245, or 250 class is a tube of that type. Such tubes will handle more input voltage than a high-μ, higher-resistance tube; they require more input voltage to deliver a given amount of power.

Distortion with such tubes is not due so much to the grid's going positive on strong signals as it is to the curvature of the characteristic at the lower end. The grid is not forced too positive but too negative, and so the negative and positive halves of the a.-c. cycle are not amplified symmetrically.

The table below shows the advantage of the 245 type of tube, delivering considerable power with a moderate plate voltage.

Types of Tube	Power Output, Watts	Plate Volts
UX 171-A	0.7	180
UX 210	1.7	425
UX 250	4.6	450
UX 245	1.6	250

213. The push-pull amplifier.—The push-pull amplifier decreases distortion caused by working a tube over a curved part of its characteristic. The curves in Fig. 164 show how the plate current curve flattens out as the load resistance in a 210 type of tube is increased.

If the current increases and decreases equal amounts above and below its average value determined by the *C* bias, all is well and good. There is no second harmonic distortion. But let us look at the curves. With the 1000-ohm load the increase is 14 ma. and the decrease is 11 ma. With a 5000-ohm load the increase and decrease are respectively 7 and 6 ma. With a 10,000-ohm load the increase and decrease are 5 ma. each. These figures indicate clearly that as the load becomes larger the inequalities between the positive and negative halves of the plate current cycle become less.

These inequalities signify that harmonics are being generated and that if a pure 1000-cycle voltage is put on the grid, the plate

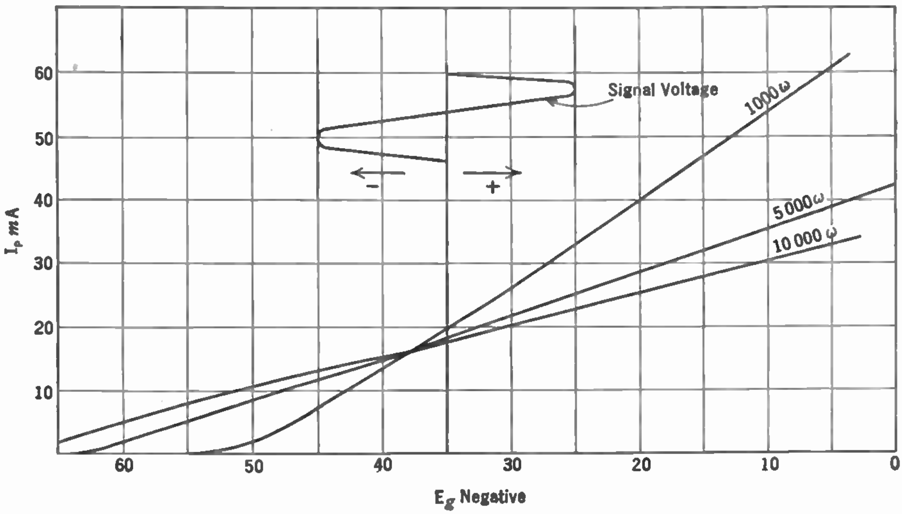


FIG. 164.—Flattening effect of increasing load resistance.

circuit will contain not only a pure 1000-cycle tone but a 2000-cycle tone as well. Distortion is being produced.

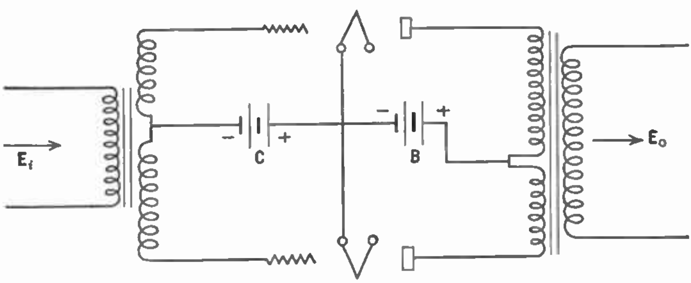


FIG. 165.—Push-pull amplifier.

The push-pull amplifier circuit is shown in Fig. 165. It consists of a center-tapped input transformer, two tubes of identical characteristics, and a transformer, or a choke, with a center tap. When a voltage is induced into the secondary winding of the input transformer one grid becomes positive a certain amount and the other grid becomes negative the same amount.

If the *C* bias, which is attached to the center of the input winding, is 35 volts and if across the entire secondary winding appears a peak a.-c. voltage of 20, one tube has its grid voltage increased by 10 volts, or to 45 volts, and the other decreased by 10 volts, or to 25 volts. Thus one plate current increases and the other decreases. These variations in a.-c. plate current flow through the output winding and may be transferred to the load. These plate circuit current variations are out of phase by 180°, one increasing, the other decreasing a like amount. One tube "pushes" current through the output, the other "pulls" current through it. Suppose both tubes pushed at the same time. What would happen? If they both pushed the same amount and at the same time no current would flow through the output winding because the two currents would neutralize each other.

If, then, we can cause the second harmonic currents to be in phase, that is, to push or pull at the same instant, and the same amount, they will not get into the load, and distortion due to these extra currents will not appear in our loud speaker. This is exactly what the push-pull system does.

Because the input voltage across such an amplifier is divided into two parts this amplifier requires twice the input voltage to give the same output power—unless the turns ratio of the input transformer is doubled, which is difficult to carry out in practice. Because of the push-pull arrangement, however, considerable overloading can be tolerated before the third harmonics which are not canceled out become objectionable. And there is another advantage—alternating current can be used to light the filaments of the tubes, with greater freedom from hum. The output transformer or choke need not have such a large core because of the fact that the d.-c. currents in the two halves are flowing in opposite directions; and since the two windings are closely coupled the resultant magnetization of the core is of a small order. Since the two windings are connected "series aiding" so far as a.-c. currents are concerned, the total inductance is increased. Not only less iron is necessary but less copper as well.

The output resistance of such an amplifier is double that of the single tube; therefore when worked into a low impedance load an output transformer must be used to see that maximum undistorted power is fed to the load. In other words the plate load must be matched to the plate resistance of the amplifier by means of an appropriate output transformer.

The output device for the push-pull amplifier may have at least two forms. Either it is a straight transformer with two windings of the proper turns ratio, or it is a center-tapped choke. At first thought one would judge that the terminals of the loud speaker would be at high voltages from each other because they are attached to the plates of the tube, but this is not the fact. It is true that they are at high potential with respect to earth or to minus *A* and so one may get a severe shock if the voltage is high and if one of the terminals of the speaker is touched by anyone who is in contact with ground. But the two ends of this choke are at the same d.-c. voltage and so no d.-c. voltage exists across the speaker. This situation, of course, prevents any current from flowing through the speaker. If one desires protection against the high d.-c. voltage from one speaker terminal to ground, he may isolate the loud speaker from the plates of the tubes by means of a condenser, but even here there are large a.-c. voltages developed, particularly when a percussion instrument in the orchestra to which one is listening is hit a sharp blow.

The push-pull amplifier, then, is a device for eliminating the second harmonic distortion which occurs when tubes are worked too far down on the curved part of their characteristic.

214. General conditions for voltage and power amplification.— In general, voltage amplification must always take place between a source of voltage in a low impedance circuit and a receiver of a voltage which is higher in impedance. The turns ratio of a transformer for the greatest voltage amplification is given by $N = \sqrt{Z_s/Z_p}$, where Z_s is the impedance into which the secondary looks and Z_p is the impedance of the transmitter. If these two impedances are equal the transformer must be a one-to-one ratio affair. There will be no step-up in voltage.

Where voltage amplification is the goal the greatest amplification will be attained when working from a very low impedance device into a very high impedance device, for example a tube with a low plate resistance working into a tube with a very high grid-filament resistance. This means that the grid of the following tube must never be permitted to go positive, for then the input resistance of this circuit becomes quite low and the amplification falls and amplitude distortion results.

Where quality of reproduction, that is, a flat frequency characteristic is desired, best results can be attained between two low impedance devices, for example a tube of low plate resistance working into a tube of low grid-filament resistance. In other words high voltage amplification and high fidelity of response are at odds, especially when it is desired to get both within a few stages of audio. One may get as much voltage amplification out of a single tube with a μ of 6 and a transformer with a turns ratio of 12 as he can out of two such tubes and a transformer with a turns ratio of 2, but in the second case he will get a flat frequency characteristic from 60 to 6000 cycles whereas in the other case he will get a characteristic that is flat nowhere, and in fact is very sharply peaked.

When one wants high amplification and high quality he must get it in several stages, and not all at once.

When one speaks of power amplification the conditions are not the same as for voltage amplification—in general. Power amplification may take place only by the aid of a tube which releases power from a set of local batteries, or from a power line. The maximum power is transferred when the impedances of the transmitter and the receiver are equal whether these impedances are high or low. But in general, power amplification implies the use of a tube which has a fairly low plate resistance which is worked into a fairly low impedance circuit or its equivalent secured by means of a transformer.

215. Power necessary for good loud-speaker operation.—In 1928 about 95 per cent of all commercially manufactured receivers used the 171 type of tube. The year 1929 saw the introduction of the 245 type and the still larger 250 type which provides a much greater margin of safety against overloading. The use of push-pull amplifiers is another step toward protection against overloading and as such is to be encouraged. In the average home push-pull 245 type tubes provide sufficient power output and a factor of safety against overloading.

216. Use of tubes in parallel.—When one cannot use power tubes of the 245 class, or when one wants more power than a single tube of any type can deliver, two tubes with grids, filaments, and plates in parallel may be used. The advantage is that the plate resistance is halved and that with a given input twice as much power output can be expected. Two 112's in parallel on 135 volts will deliver to a 2500-ohm load 240 milliwatts with a plate current consumption of 14 ma., which is within the realm of economical B battery operation.

217. Comparison of push-pull and parallel tubes.—In calculations involving push-pull and parallel tubes one uses the formulas developed in the previous chapter for voltage amplification and power output. The only difference lies in the plate resistance which is one-half that of a single tube in the parallel case and twice that of a single tube in push-pull case. Thus if two 112 type tubes are operated with grids, filaments, and plates in parallel, the plate resistance will be about 2500 ohms or about the same as that of a 171 tube. The resistance of two such tubes operated in push-pull will be 10,000 ohms. This means that an output transformer of the proper turns ratio is necessary when operating the tubes in push-pull into a low-impedance speaker if the maximum transfer of energy at some low frequency is desired. Owing to the push-pull feature of balancing out the second harmonics incurred in working a high-resistance tube into a low-resistance load, the output will be relatively free from distortion of this type. The curve in Fig. 145 shows the effect on the transfer of power of operating a tube into a load lower in resistance than itself.

If the input grid voltage is r.m.s., the following formulas give the power output when the proper turns ratio transformer is used so that the load resistance is double the resistance of the amplifier. In these formulas R_p is the plate resistance of a single tube, not of the amplifier.

(1) Single tube power output $= \dfrac{2\,\mu^2 E_g{}^2}{9\,R_p}$.

(2) Parallel tube power output $= \dfrac{4\,\mu^2 E_g{}^2}{9\,R_p}$.

(3) Push-pull tube power output $= \dfrac{4\,\mu^2 E_g{}^2}{9\,R_p}$.

Because of the greater freedom from objectional harmonics when the push-pull amplifier is overloaded, somewhat greater input voltages can be tolerated than with a single tube. It must not be supposed, however, that five or six times the power output of a single tube can be obtained without serious distortion as has been stated by some writers. It is probable that the greatest advantages of this type of amplifier lies in its ability to transmit ordinary volumes without appreciable distortion, to be operated on alternating current without appreciable hum, and to be used with plate voltage supply units in which the degree of filtering is not so great as is necessary with single-tube amplifier stages. For example with the push-pull amplifier, no a.-c. currents can get into the plate voltage supply and it is not necessary to filter the C voltage equipment so much as with a single tube.

CHAPTER XII

THE DESIGN OF AUDIO AMPLIFIERS

THE audio amplifier is at least half of the modern radio receiver. In addition to being necessary to the reception and reproduction of radio signals, the audio amplifier may be used with phonographs, talking films, public address systems, etc. The design of audio amplifying equipment forms a large part of the work of any radio engineer. This chapter gives some of the theoretical and practical work that must be understood before one can intelligently design an amplifier.

218. The transmission unit.—When one compares the voltage amplification of the power output of any system in which the ear is likely to play a part—as in an audio amplifier—it is convenient to express the greater amount of amplification, or power, which one amplifier gives over another by means of a unit that bears some relation to the sensitivity of the ear. For example one amplifier may turn into a loud speaker a power output of 800 milliwatts and another an output of 1000 milliwatts. How much difference would this make to the ear? Offhand it seems that a considerably greater volume would result. But such is not the case. Such a ratio of one power to another as 1000 to 800 is scarcely discernible to the ear.

We can state that an amplifier has a voltage gain of 50 and that under some other condition it has a gain of 60 and imagine that the latter is easily noted by the average ear. But is it?

A convenient unit of loss or gain is the **decibel**, abbreviated as **DB**, which has taken the place of the **TU**, an American unit originated in the telephone industry where nearly all calculations of power must in one way or another involve the ear. The Bel was the unit universally adopted in 1928—it is ten decibels—

and is named in honor of Dr. Alexander Graham Bell, the inventor of the telephone. The difference in two powers differing by one DB is just discernible to the ear.

The DB is a logarithmic unit—that is, each time the amount of power of a device is doubled—or multiplied by 2—we add 3 DB. When the power is increased ten-fold—multiplied by 10—we add 10 DB. Here, then, is the second advantage in the DB. We can add them, instead of multiplying them. For example let us suppose the voltage amplification of an amplifier is 25 and that it is to be connected after another similar amplifier. What is the voltage gain? Evidently, if the second amplifies what the first gives it, the overall gain will by 25^2 or 625. Here we must multiply 25 by 25, which is awkward. But if we knew that one amplifier had a voltage gain corresponding to 25 DB and was to be used after another of similar characteristics, we would state that the overall gain was 25 plus 25 or 50 DB. The DB is defined as " ten times the common logarithm of the ratio of two powers," or

$$N_{DB} = 10 \log_{10} (P_1/P_2) \tag{1}$$

in which N is the number of DB by which the two powers P_1 and P_2 differ. The table below gives some easily remembered values of DB and their corresponding power or voltage and current ratios:

N_{DB}	Approximate Power Ratio	Approximate Voltage or Current Ratio
3	2.0	1.41
4	2.5	1.59
6	4	2.0
7	5	2.24
9	8	2.82
10	10	3.16
20	100	10.0
23	200	14.1
30	1000	31.6

Let us consider an amplifier with an output power of 100 milliwatts. How much must we increase its power output before the ear can just detect the difference? Suppose we double the output. The ratio is then 200/100 or 2 and the DB corresponding to this power ratio is 3. The ear can detect one DB difference and using a table of DB or a slide rule we find that 1 DB corresponds to a power ratio of 1.25 roughly. Thus the power output to which 100 milliwatts must be increased before the ear can detect the difference is such that $P = P_2/100 = 1.25$ or 125 milliwatts. Adding another DB brings the level up to 160 mw. and another unit brings it to 200 mw., as indicated above.

In this case it would have been foolish to go to great efforts to effect an output of 115 compared to an output of 100—because the ear could not tell the difference. In fact the ear can only with some difficulty tell the difference between the amplifiers differing by 3 DB—double the power—unless single tones are used and then only in a quiet room.

219. Voltage and current ratios.—Strictly speaking the DB should be used only when expressing the ratios of powers. Let us suppose two amplifiers are feeding current into equal resistances. The currents are different. How can we express in DB the advantage of the one as a current amplifier? We need only find out the ratio of the powers as before, and multiply the logarithm of this ratio by 10. Thus,

$$P_1 = I_1^2 R$$

$$P_2 = I_2^2 R$$

$$\text{DB} = 10 \log P_1/P_2 = 10 \log \frac{I_1^2 R}{I_2^2 R}$$

$$= 10 \log \frac{I_1^2}{I_2^2}$$

$$= 20 \log \frac{I_1}{I_2} \qquad (2)$$

If the resistances are not equal (2) becomes

$$\text{DB} = 20 \log \frac{I_1\sqrt{R_1}}{I_2\sqrt{R_2}} = 20 \log \frac{E_1/\sqrt{R_1}}{E_2/\sqrt{R_2}} = 20 \log \frac{E_1\sqrt{R_2}}{E_2\sqrt{R_1}} \qquad (3)$$

The factor 20 arises from the fact that when one squares a number the logarithm is doubled. For power ratios, the DB is 10 times the logarithm, for current or voltage ratios the DB is 20 times the logarithm of the ratio.

Voltage or current ratios can be translated into DB only when the impedances into which the current flows, or across which the voltage exists, are taken into account. If these impedances are equal for both currents or both voltages, they cancel out, one being in the numerator and one being in the denominator, but in general they do not cancel out and must be considered.

The DB is always an expression for a ratio. We cannot speak of an amplifier that has an output of so many DB, but if we assign some arbitrary level—say 10 milliwatts—and compare all amplifiers to this amount of power we can say that one has 20 DB or 100 DB greater output, or less output, or is " up " or " down " 20 or 100 DB. All these DB are expressions for the ratio between these powers and the " zero " level power of 10 milliwatts.

Example 1–12. An amplifier has 1 volt applied to its input resistance of 10,000 ohms. Across its output resistance of 4000 ohms appears a voltage of 40. What is the power gain in DB? The voltage gain? Would it be worth while to increase the output voltage from 40 to 50 volts?

Solution.

Power input $P_i = \dfrac{E_i^2}{R_i} = \dfrac{1}{10{,}000} = 10^{-4}$ watts.

Power output $P_o = \dfrac{E_o^2}{R_o} = \dfrac{40^2}{4000} = \dfrac{1600}{4000} = 0.4$ watt

$$\frac{P_o}{P_i} = \frac{0.4}{10^{-4}} = 4 \times 10^3 = 4000$$

Power gain $= 10 \log 4000 = 36$ DB (because the log of 4 is 0.6 and the log of 1000 is 3 and the log of 4000 is 3.6)

Voltage gain $= 36 \text{ DB} = 20 \log \dfrac{E_o\sqrt{R_i}}{E_i\sqrt{R_o}}$

Hence $\log \frac{E_o\sqrt{R_i}}{E_i\sqrt{R_o}} = 1.8$

$$\frac{E_o\sqrt{R_i}}{E_i\sqrt{R_o}} = \text{antilog } 1.8$$

Voltage gain $= 63$

If E_o becomes 50 volts,

$$P_o = \frac{50^2}{R_o} = \frac{2500}{4000} = .625$$

The gain due to this increased output over P_o (above) is

$$\text{gain} = 10 \log \frac{.625}{.400} = 10 \log 1.56$$

$$= 2.0 \text{ DB (approximately).}$$

And so the gain due to increasing the output from 40 to 50 volts—or from 400 to 625 milliwatts—will be audible to the ear, but the difference is not worth a great deal of effort to attain it.

The solution of the above example is characteristic of the solutions of all such problems. Given the power ratio it is only necessary to look up the logarithm of this ratio to get the DB gain. The student must not forget that all numbers between 100 and 1000 have as the first digit of their logarithms the number 2. Hence all power ratios between 100 and 1000 lie between 20 and 30 DB. Multiplying any power by 10 represents a gain of 10 DB. Thus of two amplifiers having outputs of 50 and 500 watts, the latter is said to be 10 DB better than the former. A loss of 10 DB means that the power in any circuit has been divided by 10. If it is decreased or increased by 100 times the loss or gain in DB is 20 DB.

Example 2–12. A certain amplifier has a characteristic such that at 100 cycles its amplification in voltage is 8, at 1000 cycles it is 80, and at 6000 cycles, where the amplifier tends to "sing," the voltage amplification is 200. Are these differences appreciable to the ear?

Let us take the amplification at 1000 cycles as a zero level and find out how much above or below this level the other frequencies are. At 100 cycles the voltage ratio is 80/8 or 10. At 6000 cycles the voltage ratio is 200/80 or 2.5. At 100 cycles there is a loss, at 6000 cycles there is a gain. Thus,

$$\text{Loss at 100 cycles} = 20 \log \frac{80}{8} = 20 \log 10 = 20 \text{ DB.}$$

$$\text{Gain at 6000 cycles} = 20 \log \frac{200}{80} = 20 \log 2.5 = 8 \text{ DB.}$$

Such a characteristic indicates a poor amplifier. The low notes would be totally lost and high ones would overload the last tube.

Example 3–12. In a certain circuit there is a loss of 25 DB. What power ratio corresponds to this loss?

Power ratios of 10 = 10 DB, 100 = 20 DB and 1000 = 30 DB. Therefore the power ratio of 25 DB lies somewhere between 100 and 1000. The figure 2 of 25 DB tells us that the loss is somewhere between 100 and 1000 times. The figure 5 of 25 DB is 10 times the logarithm of 3.1 and so 25 DB corresponds to a power ratio of 310.

The solution of such a problem is as follows:

$$25 \text{ DB} = 10 \log_{10} \frac{P_1}{P_2}$$

$$2.5 = \log \frac{P_1}{P_2} \text{ (dividing both sides by 10)}$$

$$\frac{P_1}{P_2} = \text{antilog } 2.5$$

$$= \text{antilog } 2.0 \text{ times antilog } 0.5$$

$$= 100 \times 3.1 = 310$$

If the loss were a voltage loss of 25 DB the solution would be:

$$25 \text{ DB} = 20 \log \frac{E_1}{E_2}$$

$$1.25 = \log \frac{E}{E_2} \text{ (dividing both sides by 20)}$$

$$\frac{E_1}{E_2} = \text{antilog } 1.25 = \text{antilog } 1.0 \text{ times antilog } 0.25$$

$$= 10 \times 1.78 = 17.8$$

220. The use of the DB.—The transmission unit may be used to express any ratio of power, voltage, current, mechanical loss or gain, etc. Thus we may say that symphony orchestra has a range 60 DB in power. That is, when it is playing very loudly, fortissimo, it is 60 DB louder than when playing very softly, pianissimo. This corresponds to a power range of one million to one. In the wire circuits which carry the microphone currents from the symphony hall to the broadcast station, the weakest of the desired signals must be 40 DB above the noise in the line. The very weak passages of the orchestra are built up by local amplifiers until the currents are greater than the noise currents. The limit to the louder passages is the overloading of the amplifiers either at the hall or in the broadcasting station. And so the stronger passages are cut down.

Whenever a circuit suffers a loss in power or voltage or current, we may express that loss in DB. The frequency characteristic of an amplifier, or a loud speaker, or of a telephone line may be expressed in DB by plotting a curve in which zero level is the amplification or power output at some arbitrarily chosen frequency. Thus if we chose 1000 cycles as a reference frequency, all other frequencies are either up, down, or flat with respect to the level at 1000 cycles.

Problem 1–12. What in DB corresponds to a voltage ratio of 100? Power ratio of 100? What voltage ratio corresponds to 100 DB? What power ratio?

Problem 2–12. A current of 0.006 ampere flows through a resistance of 1000 ohms. A switch reduces this current to 1.0 milliampere. How much is the current reduced in DB?

Problem 3–12. An amplifier has a normal output of 1 watt. A switch is provided that its output can be reduced in 5-DB steps. What is the output in watts when it is reduced by 5, 10, 20, and 25 DB?

Problem 4–12. An amplifier has its power output reduced by 25 per cent. Is such a reduction in power audible to the ear?

Problem 5–12. A radio receiver has a voltage gain in its radio-frequency amplifier of 50 DB. Express this in voltage gain, and in power amplification provided that the same impedance closes the input and output of the amplifier.

Problem 6–12. A radio receiver is so adjusted that a station 20 kc. off the frequency at which the receiver is tuned is reduced by 40 DB in voltage below the station that is being listened to. What is the ratio in voltage between the desired and undesired station?

Problem 7–12. A broadcasting station increases its power from 500 to 5000 watts. What is this in DB? What is the increase if the power is increased to 50,000 watts?

Problem 8–12. If an audio amplifier has two stages and each stage has a gain of 25 DB, what can the gain of the receiver be reduced to when listening to the 50,000-watt station compared to the 500-watt station provided they are equidistant? In other words, a given station increases its power from 500 to 50,000 watts. How much audio gain in DB is this worth to the listener?

Problem 9–12. The noise on a certain telephone line is 40 DB down from the broadcasting signals. What is their power ratio? If the telephone currents are of the order of milliamperes, what are the noise currents?

Problem 10–12. Phonograph records with single frequencies are made by the Victor Phonograph Company for use as frequency standards. A certain record is labeled as being "− 2.0 TU" compared to a certain arbitrary level. What is the voltage ratio of the record compared to the arbitrary zero level?

Problem 11–12. The maximum power output from a 112 type of tube is 120 milliwatts. The 171 has an output of 700 milliwatts. How much greater in DB is the 171 power output?

Problem 12–12. A loud speaker is 5 per cent efficient and requires 1.5 watts to give sufficient volume output. If it is made 50 per cent efficient how much can the power input be reduced to give the same output?

Problem 13–12. A tube has a plate resistance of 5000 ohms. Calculate the power into a load which varies from 1000 to 20,000 ohms and convert the ratio between the power at maximum to the power at other values of load resistance in DB. How great can the difference between the load and the tube resistance be before the ear will note the difference?

Problem 14–12. The sensitivity of a condenser transmitter (high quality microphone used in better broadcast studios) is 0.35 millivolt per dyne of force exerted by an air wave impinging on each square centimeter of the diaphragm. The carbon button microphone has a sensitivity of 5.0 millivolts per dyne per square centimeter. How much more sensitive is the latter over the condenser transmitter, expressed in DB? How many stages of transformer-coupled audio amplification using 2 : 1 transformers and tubes with a μ of 8 will be required to bring the output of the condenser transmitter up to the level of the carbon button microphone? A commercial telephone transmitter—such as is used in ordinary telephones—is tuned to the average speech frequency and therefore amplifies what corresponds to its input about 1000 times. Express in DB its sensitivity compared to the other two microphones.

Problem 15–12. A radio receiver is so adjusted that its output is 8 DB above an arbitrary level. The maximum power the receiver can put out is 10 DB above this level. If the output power is proportional to the square of the power of a broadcasting station which is producing the output of 8 DB, by how much will the output tube of the receiver have to be increased in DB if the transmitter doubles its power?

Problem 16–12. A radio receiver is tuned to a certain distant station which gives at the receiver input a voltage of 500 microvolts. A nearby station on a different frequency produces a voltage of 50,000 microvolts at the same time. How much loss in DB must be put into the receiver at the frequency of the undesired station to reduce the signals to the same level? How much additional loss must be put into the receiver to reduce the unwanted station to 60 DB below the desired signal? The curves in Fig. 166 will be interesting in connection with this problem. They were published by Lloyd Espenschied in the Bell System Technical Journal, January, 1927. They show the relative selectivity of several types of receiver. The "double detection" receiver is a superheterodyne.

Problem 17–12. It is desired to make a gain control which will affect the output of a receiver in steps too small to be noted by the ear. An average

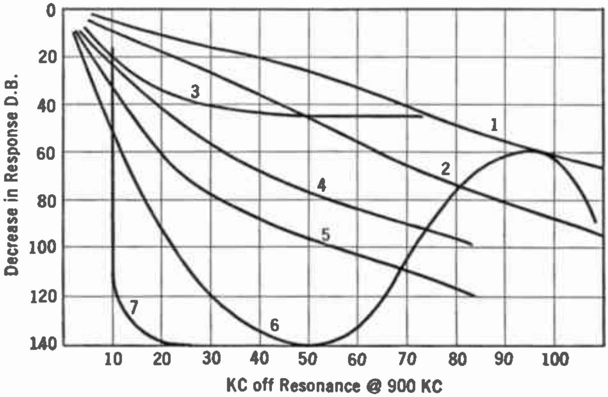


FIG. 166.—Selectivity of several circuit combinations.

1 = Single circuit non-regenerative
2 = Couple circuit non-regenerative
3 = Single circuit regenerative
4 = Tuned Radio Frequency
5 = Tuned Radio Frequency
6 = Double Detection (Super Heterodyne)
7 = Ideal Characteristic

person will readily note a change of volume of 3 DB in the middle of the audio-frequency band, but changes of 10 DB at the extreme upper and lower frequencies are not noticed. Suppose the loud speaker has an impedance of 4000 ohms, and that the gain control is to be placed across it—where it should never go! What shunting resistance will be necessary in the gain control so that the changes in volume will occur in steps too small to be noticed? The gain control has a maximum value of 20 DB.

Problem 18–12. The ratio of peak power in the voice (accented syllable) to average may be 200 to 1. Thus if the average power is 10 microwatts, the peaks may be as high as 2000 microwatts. Express the range in power of the human voice in DB?

221. Design of audio amplifiers.—There have been two schools of thought regarding the design of radio equipment, especially the part of the radio set that follows the detector or demodulator, the audio amplifier. Should each unit be made so that its frequency characteristic and voltage or power gain may be as good as possible, or should the entire amplifier have the characteristics desired by permitting some faults in one part of the circuit to be corrected in another? As long as parts are obtainable so that the experimenter or the service man can construct his own amplifier, he must face this problem. But a manufacturer who is not interested in selling transformers by themselves, but who is interested in an amplifier which from its input to its output shall have certain characteristics, need not worry about individual stages. What he wants is the end product to be as he has planned. It is obviously unwise to let faults creep into one stage that must be corrected in another if the correction is more difficult than to design the individual stages units carefully in the first place, but it is equally unwise to take great pains to make individual stages perfect when minor faults in one can be easily corrected in another.

The amplifier designer, then, is interested in the ratio of what he gets out to what he puts into his amplifier, both as regards quantity and quality. He must, of course, have an eye on his individual units as well as on the amplifier as a whole. Let us begin, then, at the detector or input to the amplifier and work toward the loud speaker, which we assume is the device into which the amplifier works.

222. Transformer working out of high impedance.—Some manufacturers make transformers of different ratios, usually two, a low ratio to work out of a detector, and a higher ratio to work out of the first audio tube. Why is this?

A tube has a lower plate resistance the higher the voltage on its plate and the lower the negative voltage on its grid. A 201–A type tube operating as an amplifier under normal conditions, that is, 90 volts on the plate and minus 4.5 on the grid, has a resistance of about 12,000 ohms. A detector tube usually has a much higher plate resistance because the plate voltage is lower. The normal detector plate voltage is 45 although many detectors are operated with but 22.5 volts on the plate. In addition many detectors, of the C bias type, have large negative biases put on the grid. The result is that instead of a resistance of 12,000 ohms out of which the amplifier must work there is a resistance of from 20,000 to 40,000 ohms.

We have already seen that a large part of the a.-c. voltage in the plate circuit of a tube will be usefully impressed on the load resistance if that resistance is several times the tube resistance. If we couple the detector tube to the amplifier through a resistance, say of the order of 100,000 ohms, we shall impress a good share of the detector plate a.-c. voltage on this amplifier—and it will be more or less independent of frequency. But if we use a transformer which is a complicated combination of inductance, resistance, and capacity, the tube and transformer will have a frequency characteristic which shows little amplification at low frequencies, high at middle frequencies and little again at high frequencies unless we are careful to get the correct circuit constants.

A transformer to work out of a high impedance and to give a good characteristic from 100 to 5000 cycles must have a greater primary inductance than a transformer which will work out of a lower impedance. The following are the reasons why such a transformer has a low turns ratio. The number of turns that can be placed on a secondary without increasing the distributed capacity to a prohibitive figure is limited. This means that the turns ratio is controlled entirely by the number of turns on the primary. Increasing the number of turns to get a high inductance decreases the turns ratio. The next transformer, on the other hand, works out of an amplifier tube, and hence out of a lower resistance. Its primary turns can be reduced somewhat and still give a good frequency characteristic, and so the turns ratio will be somewhat greater. The Amertran DeLuxe transformers have ratios of 3 to 1 and 4 to 1 for the first and second stages. The Sangamo Type A transformers, on the other hand, are of 3 to 1 ratio and can be used for either first or second stage. Both sets of transformers give very good frequency characteristics. Of two transformers, choose the one with the highest primary inductance for the first stage. This will be the lower ratio transformer.

223. Rules for the amplifier designer.—In general the rules the amplifier designer must follow are these:

1. He must so design the amplifier that no stage can overload even on the strongest signals that are to be received. This implies that each tube has its proper C bias and plate voltage.

2. In the plate circuit of each tube must be a sufficient impedance that at low audio frequencies the characteristic is straight and not curved. This implies that the E_g–E_p curve for a circuit may be one thing for 1000 cycles and another for 100 cycles—which is correct when apparatus is used that has reactance. At 1000 cycles the tube works into one impedance—at 100 cycles into a much lower one.

3. He will get a better characteristic—although less gain—from low impedance, low μ tubes. This will require more tubes, of course, to get a predetermined amount of amplification.

4. He will get more amplification—but a poorer characteristic with high-μ, high-impedance tubes.

5. The more tubes in the amplifier, the greater will be the noise in the output due to "tube noise." One well-known physicist-engineer has stated that the proper place for the loud speaker is in the detector circuit.

6. The more tubes and the higher the overall gain of the amplifier the greater will be troubles from instability and from unwanted pickup from nearby a.-c. magnetic fields.

These are general rules and statements, and it will not pay to be dogmatic about them. They may work in some instances, and fail in another.

The maximum voltage amplification that can be secured from a transformer-coupled stage is μ times the turns ratio of the transformer. If the impedance into which the tube works—the *reactance* of the primary if the secondary is open-circuited—is two times the plate resistance of the tube, 89 per cent of the μ of the tube will be realized. If the impedance of the transformer at the lowest frequency it is desired to amplify is two times R_p, the amplification at this frequency will be 75 per cent of the maximum possible, and nearly 100 per cent of the maximum possible will be attained at all frequencies. Then the range in amplification will be from 89 per cent to 100 per cent at all useful audio frequencies. The difference between these values of amplification will not be audible to the ear.

224. Comparisons between amplifiers.—The only fair test between two amplifiers is made by means of a switch which alternately throws one set-up and then the other to the detector tube or phonograph pick-up being used. A test on one amplifier at one time and a test on another at some different time is no test at all. The music may be different, the mood of the listener may be different, and there are too many other variables to give any faith in such a test. A simple four-pole double-throw switch will throw the amplifiers to the input and to the loud speaker with but a second's delay.

The engineer must remember that the ear can scarcely detect volume differences in which the power ratio is 2 to 1 and that, at the two extremes of the audio-frequency range, differences in power of 10 to 1 are none too easily noted. To spend great effort and much money in making an amplifier flat from 50 to 5000 cycles is not usually warranted by the difference in fidelity noted by the ear over an amplifier that is down 10 DB at the two ends.

225. Volume control.—The volume of a radio set is seldom controlled by doing something to the audio amplifier. The volume control is usually before the detector tube, in order that this tube shall never overload. Such a volume control may go into the antenna-ground circuit at the very beginning of the signal's path through the receiver. Or it may come in one of the radio-frequency amplifiers or even in the input to the detector. Study of detection indicates that less distortion will result if this input to the detector is kept at some constant desired level.

In 1929 it became necessary to develop new means of controlling volume. Many designers not only reduced the voltage amplification to reduce volume but at the same time reduced the coupling to the antenna. Some reduced the gain of the audio system too so that the hum inherent in an a.-c. operated set was reduced simultaneously with the volume of desired signals.

If the amplifier is used with a phonograph pick-up, some means of controlling volume may be necessary. Such a control may be a variable resistance across the secondary of the first transformer as shown in Figs. 167 and 168. This has the effect of lowering the turns ratio of the transformer, and therefore permits only part of the total available voltage to get to the grid of the amplifier tube.

The usual output voltage of a phonograph pick-up is of the same order as that from a detector tube, that is, from 0.1 volt to perhaps 1.0 volt. If the lower value, some additional amplification may be necessary to get the desired volume, and then a means may be provided whereby the pick-up voltage is impressed on the grid of the detector tube which is then used as an amplifier, or another additional transformer or complete stage may be thrown into the circuit as desired.

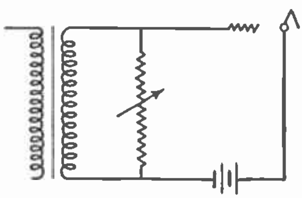


FIG. 167.—Shunt resistance volume control.

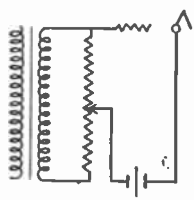


Fig. 168.—Potentiometer gain or volume control.

226. Proper C bias for power tubes.—The proper value of *C* bias for an amplifier tube is determined partly by the input voltages to be encountered and partly by the amount of d.-c. power the plate can dissipate safely. This power is the product of the plate voltage and the plate current, and the latter is controlled to some extent by the *C* bias.

Problem 19–12. A power tube's plate current is as follows,

E_p	E_c	I_p, ma.
450	0	100
	20	55
	30	35
	40	18

and the maximum safe power that can be dissipated at the plate is 10 watts. What is the minimum value of grid bias (E_c)?

227. Loss in output transformer.—With the advent of large power tubes of the 171, the 210, and the 250 types, the necessity of using two or more tubes in parallel has ceased, so far as the average experimenter or set designer is concerned. To get considerable power output, it is advisable to use the largest tube ordinarily employed in receivers, namely, the 250 type, instead of using several tubes in parallel. If still greater power is required—and the 250 will turn out nearly 5 watts of audio-frequency power—several power amplifier stages may be operated in parallel and connected to whatever load they are to drive.

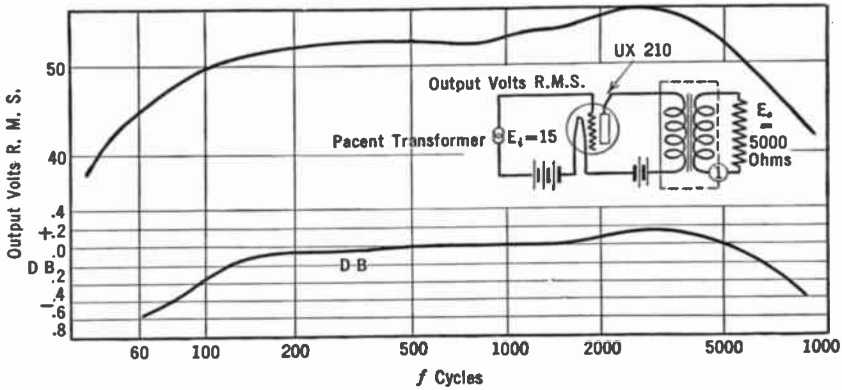


Fig. 169.—Transmission characteristic of output transformer.

A single 250-tube amplifier worked up to its limit would provide sufficient power for about five loud speakers running at considerably above normal output for average apartment volume level. For each five apartments, then, another 250-tube amplifier could be installed and driven from the next-to-the-last stage of audio in the equipment.

Difference in impedance between the tube and the equipment into which it works can be taken care of by means of the output transformer. The curve in Fig. 169 shows the transmission characteristic of a Pacent 1 : 1 output transformer designed to work out of a 210 type or 5000-ohm tube. The loss in power transmission occasioned by the transformer is small, and the distortion due to its own frequency characteristic will not be noted by the most critical ear.

228. Turns ratio in output transformers.—When there are large impedance differences between tube and loud speaker, a transformer must be used.

For example the average dynamic type of loud speaker has an input impedance of from 5 to 10 ohms whereas the lowest resistance tube in common use is the 171, 2000-ohms. Hence an output transformer is necessary to provide maximum energy transfer from the tube to the speaker. The turns ratio for such a loud speaker working out of 5000 ohms would be about 25 : 1.

The turns ratio should be such that the tube always works into an impedance greater than its own plate resistance, in order to minimize curvature distortion and its accompanying second harmonics. This means the turns ratio can be somewhat less than that necessary to "match" the tube and speaker at the lowest frequency to be received.

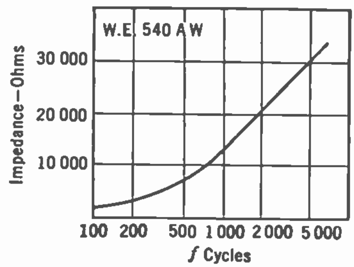


FIG. 170.—Impedance of cone type loud speaker.

The Western Electric 540–AW speaker, as shown in Fig. 170, has an impedance of about 1500 ohms at, say, 100 cycles, and thus to couple it to a 2000-ohm tube requires a step-down ratio of 0.87 for maximum power transfer.

229. Manner of coupling tube to load.—Output devices are used to

(1) Keep d.-c. current from the loud speaker winding;
(2) Prevent serious loss in plate voltage;
(3) Prevent heating the loud speaker winding by the plate current of the last tube;
(4) Prevent placing a mechanical bias on the loud speaker armature or moving element;
(5) Adjust serious impedance differences between tube and speaker, and therefore to improve fidelity and increase power;

and some output devices

(6) Keep the loud speaker terminals at low d.-c. potentials and prevent shock or burn.

There are two types of output devices. The transformer proper having two windings insulated from each other is one type; another is the choke-condenser device. The choke consists of a large number of turns of copper wire on an iron core. The condenser is an ordinary filter or by-pass condenser preferably of about 2–4 mfd. capacity. The choke should not be smaller than 12 henrys.

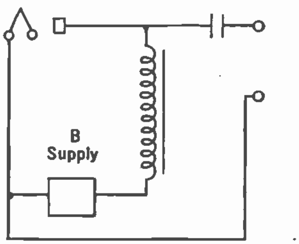


FIG. 171.—In this output connection, loud-speaker currents return to the filament directly.

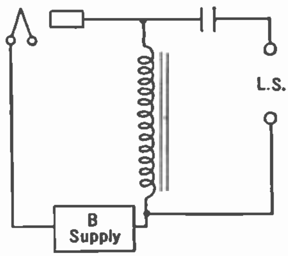


Fig. 172.—Here the loud-speaker currents must flow through the *B* supply to return to the filament.

The transformer by its very nature keeps d.c. from the loud speaker. Its primary d.-c. resistance is small and so serious loss in plate voltage is not experienced.

The choke-condenser also keeps d.c. from the loud speaker because of the condenser. If the choke is tapped, impedance differences may be adjusted.

The choke-condenser may be connected into the circuit in two ways, one of which is much better than the other. In one connection, Fig. 172, the circuit is the same as the output transformer in that all of the a.-c. currents in the plate circuit of the last tube must return to the filament of this tube by going through the plate voltage supply device, whether batteries or an "eliminator." In the other connection, Fig. 171, the a.-c. plate currents in the loud speaker return directly to the filament and do not go through the plate voltage supply device. This is a distinct advantage as will be seen in Section 230.

The equivalent circuit as far as a.c. is concerned is shown in Fig. 173. The choke represents a shunt Z_L across the tube and loud speaker, and to prevent loss in power it must be large in impedance compared to the loud speaker. The condenser, in series with the loud speaker, represents a series loss Z_c and must be small in impedance compared to the loud speaker impedance. The loss may be calculated by estimating what power would get into the loud speaker if the condenser and choke were not present, and then calculating what power would be transmitted if either or both of these additional units were present.

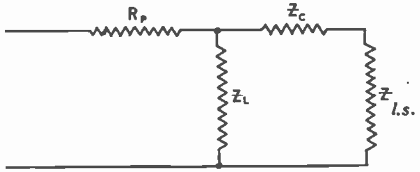


FIG. 173.—The equivalent circuit of Figs. 171 and 172.

Problem 20–12. A 171 type tube is to feed power into a speaker which at 200 cycles has an impedance of 2000 ohms. The 171 has a plate resistance of 2000 ohms. The condenser is 4 mfd. and the choke is 20 henrys. Calculate the loss in DB of having the choke present, of having the condenser present, of having both present. What would be the losses if the choke were only 10 henrys, and the condenser only 1 mfd.? (Neglect phase in calculations.)

230. Method of connecting choke-condenser.—What difference does it make which way the loud speaker is connected to the choke-condenser? Let us consider in Fig. 174 a typical case, a two-stage transformer-coupled amplifier and a detector getting plate voltages from a common source; the box labeled "B supply." Let us suppose an a.-c. voltage of 50 appears across the choke at a frequency of 1000 cycles due to an amplified voltage of this frequency coming from the detector. This voltage will cause an a.-c. current of about 0.2 ma. to flow through this inductance, which presents an impedance of about 250,000 ohms to the 1000-cycle voltage. To get back to the negative side of the filament of the last tube this current must flow through the impedance of the B supply, which for purposes of argument is about 80 ohms (the impedance of a 2-mfd. condenser to 1000 cycles).

This current through 80 ohms impresses 0.016 volt on the primary of the first audio transformer in series with the plate resistance of the detector tube. Most of this voltage will appear across the transformer, and will be amplified to reappear finally across the output choke. If the transformer windings are poled correctly and if there are three stages getting plate voltage from the common supply, this voltage will reappear across the output choke in phase with the 50 volts already mentioned.

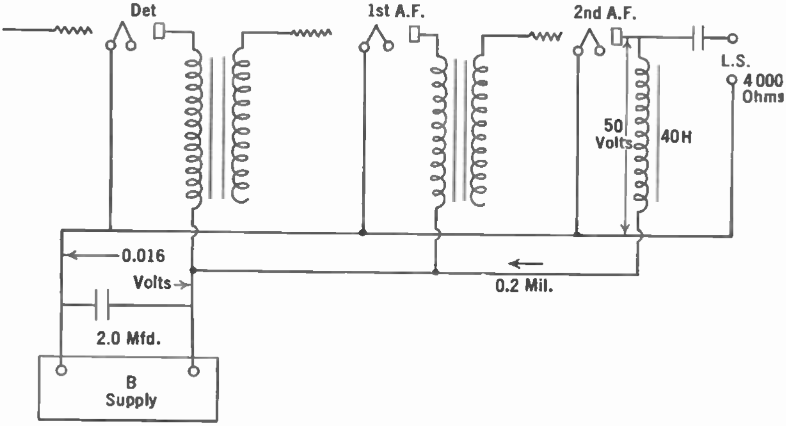


FIG. 174.—The proper output connection.

Let us suppose, now, that the loud speaker is connected directly across the choke, as in Fig. 175. If this speaker has an impedance at 1000 cycles of 4000 ohms, the effective load in the plate circuit of the tube is 4000 ohms shunted by 250,000 ohms, or not far from 4000 ohms, neglecting phase angles. Now the 50 volts a.c. across this load will produce a current of 12.5 ma. which will flow through the 2-mfd. condenser and produce 1 volt across it which will be amplified and return across the load in phase as before. If the voltage gain of the amplifier from primary of the first transformer to the voltage across the load is 200, the returning voltages in the two cases will be 2.1 and 125 volts, respectively. In the second case the amplifier will " sing " because enough of the voltage across the output is impressed back again on the input and amplified enough to return greater than the original voltage. In the first case the returning voltage is less than the original voltage, and after a cycle or two of going through the amplifier the returned voltage will die out.

The advantage is clearly with the connection which returns the loud speaker currents directly back to the filament of the final tube and which keeps them out of the B supply. The output transformer does not have this advantage. The push-pull amplifier

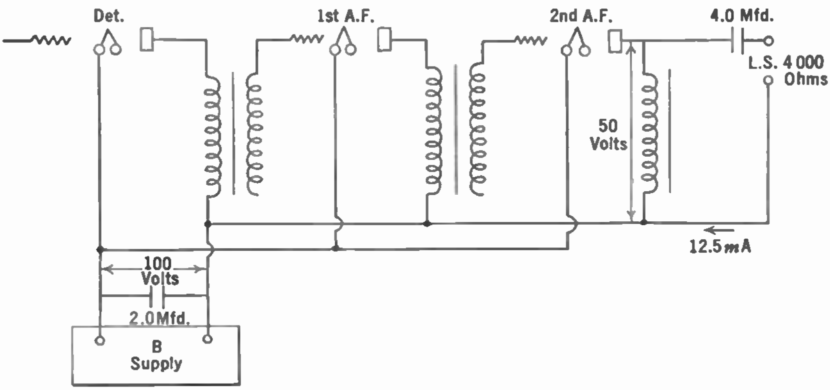


FIG. 175.—Regeneration in audio amplifiers is caused by forcing a.-c. currents through the impedance of the B supply.

keeps a.-c. currents out of the B supply and is more stable for that reason.

231. Voltage limits on the output condenser.—In case the loud speaker is connected across the choke the voltages the condenser must stand are only the a.-c. voltages existing across the choke because the d.-c. voltage across the choke is small. On the other hand, if the loud speaker is connected from the condenser to the filament as in Fig. 174 the voltages across the condenser are not only the a.-c. voltages but the steady d.-c. voltage on the plate of the last tube as well. It must be a better condenser in this case. If the B voltage is 180, the condenser should be able to stand up under occasional surges of twice this value. Its rating should be 400 volts. If it blows up, the loud speaker will probably be ruined because the entire plate battery voltage of the last tube will be impressed on the speaker and the choke in series.

If the condenser in case of Fig. 172 blows up, nothing happens —the choke will have a lower d.-c. resistance than the loud speaker and most of the current to the tube will go through it in preference to the speaker.

232. Regeneration in audio amplifiers.—The troubles from regeneration in audio-frequency amplifiers have been largely overlooked. The simple case cited in Section 230 where the loud speaker currents went through the impedance of the B supply device and were impressed back upon the input to the amplifier is but one example. The case cited below presents some laboratory data on just what happens when regeneration exists. A.-c. currents in an audio amplifier must be returned directly to the filament of the tube they are generated in, and never permitted to roam around through the wiring, through the B supply device, through the *C* bias resistor, etc. Otherwise, regeneration cannot help being sometimes helpful, sometimes harmful; since it is never predictable it is best to prevent it.

Regeneration occurs when any impedance is common to two amplifier circuits. Currents from one circuit set up a voltage across this impedance. If this voltage is impressed upon a previous amplifier circuit, regeneration takes place. Coupling may take place across a resistance, a condenser, a coil, or across any complex combination of these three components of impedance.

233. A case of regeneration.—A two-stage transformer-coupled amplifier employing Amertran DeLuxe transformers was built and proper means taken to prevent a.-c. currents from one circuit causing trouble in another. The circuit diagram is given in Fig. 176. The *C* biases for the two tubes were obtained by the plate current of the tubes in question flowing through 2000-ohm resistors R_2 and R_6. To prevent any a.-c. voltage which might appear across these resistors from getting into the grid or input circuit of the tube, the grid circuits were filtered by a large capacity (1 mfd.) across the resistor C_2 and C_4 and two high resistances R_3 and R_5 in series. Since no d.-c. current flows in this circuit there is no loss in d.-c. voltage. The *C* bias is determined by the size of the resistance and the plate current flowing. The values of bias are immaterial for our present discussion.

The plate voltages for the first and second tubes corresponding to detector and first audio tubes were obtained by reducing the voltage on the power tube by series resistances R_1 and R_4 in this case from 180 volts to 90 and 45.

A.-c. voltages were fed into the amplifier through a 12,000-ohm resistor to simulate the resistance of a previous tube. The current into 4000 ohms was read. The input was constant at all frequencies and under all test conditions. If the output meter did not change,

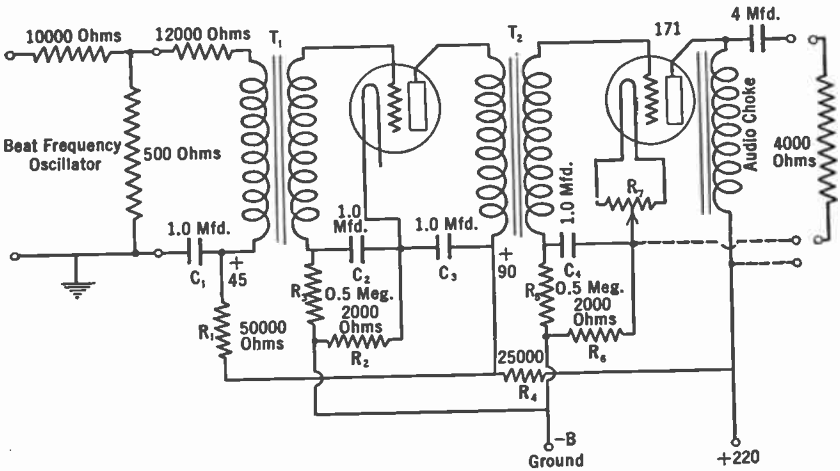


FIG. 176.—A high quality, well-filtered audio amplifier.

the characteristic of the amplifier was flat. If it did vary, the changes were indicative of the gain or loss in amplification at the frequency then being used. We are not concerned with the amount of amplification now, we are interested only in the characteristic obtained. The B supply device was a Majestic B eliminator using a gaseous rectifier tube.

When all the filtering was in the grid and plate circuits and the loud speaker was connected so that the a.-c. currents were fed back to the center of the last tube's filament and thus were kept out of the B supply (as in Fig. 176), the characteristic was flat from 100 to 8000 cycles, was down only 1 DB at 60 cycles, and was up 8.6 DB at 10,000 cycles where the transformers were going resonant (A) Fig. 177.

Removing the filtering in the detector plate circuit so that the 45-volt supply came directly from the eliminator dropped the 60-cycle response 6.6 DB (B). Removing the filtering in the grid circuit of the first tube had no effect on the low frequencies and reduced the peak around 10,000 cycles. Getting the 45-volt supply from the B supply directly (unfiltered), removing the grid filter resistors (0.5 megohm) by-passing the plate resistors, reduced the output at 60 cycles by 6.5 DB; placing the loud speaker across the output choke and keeping other conditions the same as the last reduced the 60-cycle output by 15 DB (D); and placing 8 mfd. across the B supply from minus to plus 180 brought up the 60 response from the last reading so that it was only 12.8 DB down from the normal output.

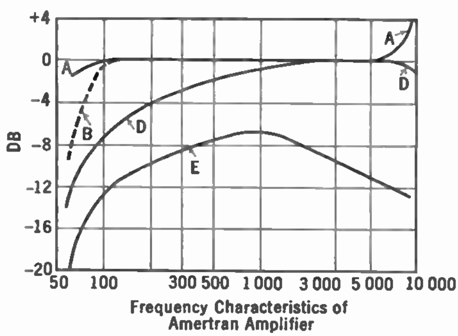


FIG. 177.—Effect of filtering the audio amplifier of Fig. 176.

With all of the filtering in the circuit, a resistance of 1000 ohms in series with the B supply had no effect on the characteristic, proving that if the amplifier is properly filtered its characteristic is independent of the B supply impedance. Without such filtering the inclusion of 1000 ohms would distort the characteristic a great deal and probably make the amplifier sing.

With no filters at all and the loud speaker directly across the output choke the response at 60 cycles was down 20 DB (E) By-passing the C bias resistor for the last tube by 1 mfd. brought the output at 60 cycles up so that it was only 16.6 DB below normal, showing that some of the a.-c. voltage across this resistor was reduced by the 1 mfd. condenser, but that the reactance of the latter was still appreciable compared with the resistor, 2000 ohms. To keep all of the a.-c. voltage out of this circuit the capacity would have to be much greater than 1 mfd.

In another case by-passing the *C* bias resistor in the first audio stage brought up the response of a two-stage amplifier over 6 DB at 6000 cycles. A.-c. voltages across this resistor were fed into the tube so that they were out of phase with the voltages there due to the grid input and, of course, detracted from the output at this frequency. This case was one involving the resonance condition where the capacity across the secondary resonated with the leakage inductance of the transformer so that a large a.-c. current went through the *C* bias resistor. When this resistor was by-passed its impedance to 6000 cycles was reduced and so the out-of-phase voltage set up there and introduced into the circuit was decreased, bringing up the output of the amplifier at this frequency.

Whether or not such resistance should be by-passed depends upon conditions, and upon amplifiers. Sometimes the characteristic might be improved—but in general it would not. It is safer to keep a.-c. currents where they belong and to use good filtering at all times.

234. Filtering in audio amplifiers.—A filter in an audio amplifier, as indicated in the last section, is designed to keep out of a certain circuit a.-c. currents of a certain frequency or frequencies. Let us look at grid circuit of the first tube in Fig. 176. Plate current flowing through the resistance R_2 causes a voltage drop. This drop is utilized as the *C* bias for the tube. If a.-c. currents flow through the resistance, they, too, cause a voltage drop, and since this resistance is now part of the grid circuit the voltages are impressed on the grid. Since the plate and grid a.-c. voltages are out of phase, these unwanted voltages getting into the grid circuit from the plate circuit cause a reduction in the amplification.

If the inductance in the plate circuit is 100 henrys and the frequency is 100 cycles, the current through the 2000 ohm resistance R_2 will be such that for every volt across the inductance there will be 0.032 volt across the resistor. This voltage is impressed on the grid of the tube and if multipled by 8 will reappear in the plate circuit as though coming into the system from the outside via the transformer. Thus a 25 per cent reduction in output will occur. This is a loss of 2.0 DB in voltage.

Now this loss may be reduced by by-passing the resistor so that the impedance offered to 100-cycle currents is smaller and so the voltage there will be smaller. A 1 mfd. condenser C_2 has a reactance of 1600 ohms at 100 cycles and when placed across this resistor will reduce the voltage there by a ratio of 2000 to 1250. Much greater isolation of the grid circuit will take place, however, if a high resistance R_3 is placed in series with the grid and a by-pass condenser C_2 is placed as shown in Fig. 176. Still greater isolation and freedom from unwanted coupling will occur if the plate circuit is filtered too, either through a resistance R_4 or through a low-resistance, high-reactance choke and, of course, a condenser C_3. Such filtering prevents a.-c. current from flowing through the C bias resistor. Grid-circuit filtering reduces the effect of such a.-c. currents as do get into C bias resistors.

In all such circuits, and indeed in radio-frequency amplifiers, too, the a.-c. currents in the plate should be returned directly to the filament of the tube in question. They should not be permitted to go back through any part of the B supply or even through the leads to it. The condenser should be a part of the amplifier, and the choke or resistor may be a part of the B supply, although it is preferable to have it in the amplifier itself. Then the amplifier is forever independent of its source of plate voltage.

The purpose of the series impedance in such filter circuits is to impose a high series loss on any a.-c. voltages or currents that may try to get into the grid or out of the plate circuit. The purpose of the condenser is to provide a low loss shunt path for these same voltages or currents to get to the filament. Any a.c. current that gets through the resistance or choke must be very greatly attenuated and on arriving at the grid end of such a series impedance it finds an easy path to the filament which is at ground potential, and therefore does not affect the plate or grid as the case may be. In case of plate filtering, a.-c. currents find an easy path to the filament through the condenser and a high impedance path to the B supply.

Such a filter is helpful in keeping any hum at 60 or 120 cycles from getting into the amplifier from the B supply.

235. Individual transformer characteristic.—An audio-frequency transformer may be looked at as a simple series circuit which may go resonant at some one or more audio frequencies. Such a transformer is never perfect; it has some primary and secondary resistance, which consumes power and puts losses into the system, and there is always some magnetic leakage (Section 64) even though this may be reduced to a very great extent by using high permeability cores, etc. The secondary resistance and leakage inductance may be transferred to the primary circuit, theoretically, and for purposes of analysis, by simply multiplying

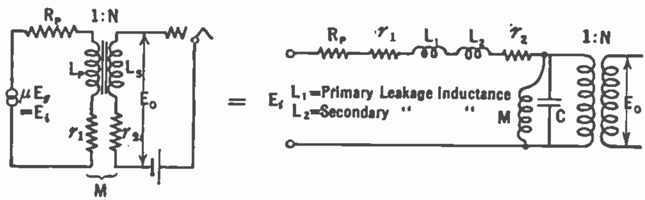


FIG. 178.—Equivalent circuit of transformer.

them by $1/N^2$ where N is the turns ratio of the transformer. The transformer then looks like Fig. 178 in which are the series resistances R_p, r_2 and r_1, and leakage inductances L_1 and L_2 and the shunt mutual inductance M—which should be very high—shunted by the capacity C of the tube and the windings, and followed by a perfect transformer which only serves to give the proper turns ratio N. If the mutual inductance—coupling between primary and secondary—is very high, it may be neglected in the following analysis of why a transformer characteristic goes up at high frequencies.

If the series inductances, caused by magnetic leakage, and the capacity C form a series resonant circuit, a voltage input E_i of this resonant frequency will build up a high output voltage E_o. This resonant peak varies from 4000 to 9000 cycles in transformers usually used in audio amplifiers. The greater the distributed capacity plus tube capacity across the secondary of the transformer, the lower in frequency is this peak. If the series resistances, due to primary and secondary resistance and other losses, is low enough the "Q" (Section 125) may be high enough for the circuit to oscillate at this resonant frequency, or to sing, as amplifier engineers say. Since the plate resistance of the tube is part of the series resistance, any decrease in R_p through use of a low-resistance tube will increase the tendency to peak or to sing at the high resonant frequency. Such a rise at the high-frequency end of the audio band may be seen in Fig. 161.

So much for the high audio frequencies. What happens at low frequencies? At low frequencies the series leakage inductance is not of importance because of the low impedance to low frequencies. The ratio between the tube plate resistance and the mutual reactance of the transformer, which is large, determines how much of the low-frequency voltage generated in the plate circuit of the tube is usefully applied to the transformer. If the plate resistance is high, or the mutual reactance is low—a poor transformer—the low frequencies will be largely lost in the tube and will not be impressed upon the amplifier. If the capacity across the transformer resonates with this mutual inductance another peak may occur in the response characteristic of the tube and transformer. This peak will be at a low frequency, and in some cases may occur as low as several hundred cycles. After this resonance occurs, there is a tendency for the response to fall off, and in some poorly designed transformers a rapid rise in amplification at say 500 cycles is followed by an equally rapid drop beyond 1000 or 2000 cycles. This tendency to drop off at high frequencies is usually overcome by the tendency to rise due to series resonance between the capacity and the leakage inductance. Making the plate resistance of the tube very high drops out all the low frequencies.

Some tricks can be played with individual transformer circuits to change the response. For example a resistance in the secondary circuit, either next to the grid or next to the filament (a C bias resistor for example) will drop off the high-frequency response. If next to the filament, as is customary for C bias requirements, the current through the capacity of the secondary of the transformer flows through the resistance and sets up an out-of-phase voltage there which may cut down the high-frequency response considerably.

236. Comparison of push-pull and single tube.—Figure 179 shows the result of a laboratory test to determine the amounts of power from a single 210 type of tube compared to push-pull tubes. It will be seen that when the grid current begins to flow, the power output begins to drop off, and that the push-pull tubes de-

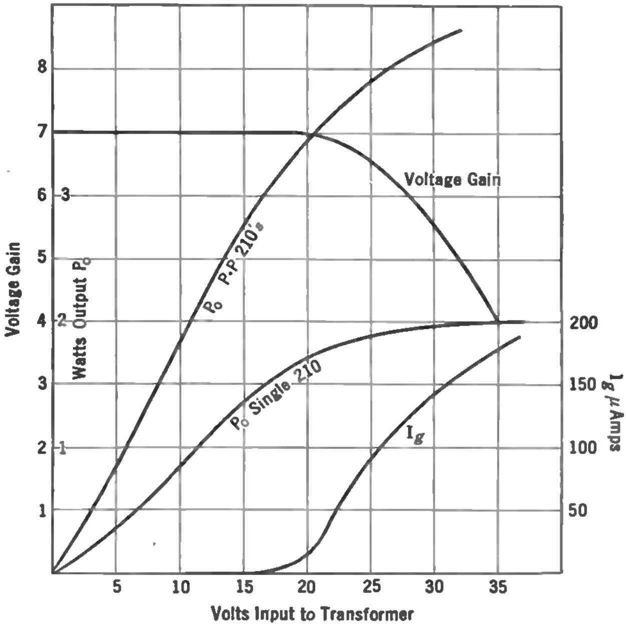


FIG. 179.—Comparison of single and pushpull tube amplifiers.

livered roughly twice the power that a single tube did. These tubes were fed through an input transformer, and the effect of grid current flowing through the secondary winding was the cause of the larger part of the distortion appearing in the curves. When the output power is no longer proportional to the input voltage squared, distortion results. The output is no longer proportional to the signals then, and larger inputs do not result in equal amounts of increase in output power. The push-pull amplifier can tolerate

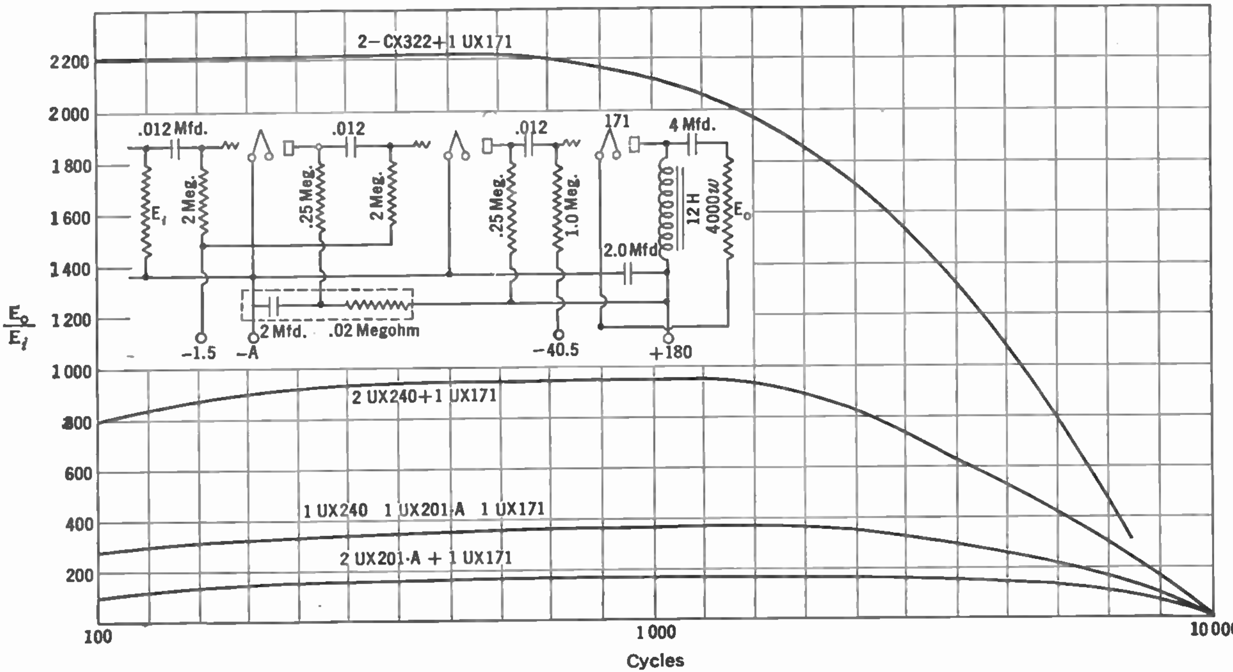


FIG. 180.—Circuit and characteristic of resistance coupled amplifier. The dotted part of the circuit is an "anti-motor-boating" device.

somewhat greater input voltages before the distortion reaching the loud speaker becomes too apparent. In other words the push-pull arrangement raises the overloading limit somewhat, but two tubes in push-pull will not deliver four or five times as much undistorted power as a single tube. The great advantage is quietness and freedom from filtering bother.

237. Screen-grid audio amplifier.—Screen-grid tubes can be used in audio amplifiers provided high impedances are supplied for the tubes to work into. This means that the use of high resistances as coupling units is essential. To determine the relative advantage of screen-grid tubes compared to high-μ tubes, etc., the circuit shown in Fig. 180 was set up, and the output voltage measured as a constant input voltage at varying frequencies was supplied to the amplifier. The result is shown in Fig. 180. The 0.02-megohm and 2.0-mfd. condenser in dotted lines is an " anti-motorboating " circuit to keep the amplifier stable when operating it from a high-resistance source of plate voltage. It is a filter to keep the a.-c. currents in their proper paths.

The " Loftin-White " circuit is a means of utilizing the high-voltage gain of a screen-grid tube as an audio amplifier. It is so arranged that the screen-grid tube looks into the high impedance input of the next tube, usually a power tube. It is a so-called " direct coupled " amplifier, meaning that the condenser in the ordinary resistance coupled amplifier is done away with, with consequent gain in fidelity. Rather elaborate precautions are taken to prevent the amplifier from being unstable, rather high voltages are necessary, but a high gain, flat characteristic amplifier requiring but small expense and space results.

CHAPTER XIII

RADIO-FREQUENCY AMPLIFIERS

THERE are three basic qualities which must be weighed not only by the designer of a radio receiver but by the purchaser and ultimate user as well. These are the **sensitivity**, the **selectivity**, and the **fidelity** of the receiver. The sensitivity of a receiver is an indication of the overall amplification from antenna-ground binding posts to loud speaker. A receiver that is very sensitive requires but a small input voltage to deliver considerable output power. The selectivity of a receiver is an indication of its ability to discriminate between wanted and unwanted signals. An infinitely selective receiver would be one that would respond only to a given station and not at all to another no matter how powerful this undesired signal was, nor how close in frequency it was to the desired signal. That there is no such receiver goes without saying. The fidelity of a receiver tells how well it reproduces what takes place in the broadcasting studio. If a certain voltage at 100 cycles is set up in the broadcasting studio, then an equal amount of 100 cycles should come out of the receiver, no more and no less. The same should be true at 1000 and at 10,000 cycles. In other words a receiver that delivers a perfectly faithful signal is one which has a perfectly flat audio-frequency response curve from antenna to loud speaker input. It has a high degree of fidelity.

A receiver that is perfectly selective, infinitely sensitive, and delivers a perfectly faithful signal is impossible to obtain. A receiver which is selective and sensitive enough for practical purposes, and the frequency curve of which is so good that the ear would not detect its infidelity is not difficult to design, to build, or to operate.

The sensitivity and selectivity are controlled almost entirely by the radio-frequency amplifier, which also has something to do with the fidelity of a receiver although this should really be a function only of the audio amplifier.

238. Purpose of radio-frequency amplification.—The radio-frequency amplifier serves one primary purpose, which is to obtain sufficient amplification to make up the enormous loss in power between the transmitting and the receiving stations. It may also be useful in obtaining selectivity, although it is not necessary that selectivity and sensitivity be interrelated.

In the majority of receivers in common use, sensitivity and selectivity are gained at the same time, and with the same apparatus, and a set that is very sensitive is usually very selective. The fact that the fidelity of the receiver, which is usually considered only as a function of its audio amplifier, may suffer considerably at the hands of the radio-frequency designer and is seldom independent of selectivity and sensitivity, is a fact that is generally overlooked.

239. Field strength.—The voltage that is set up across a receiving antenna is called the **field strength** of the transmitter at that particular point on the earth's surface. It is usually of the order of millivolts, and because a higher antenna will pick up a greater signal—that is, the voltage across it will be greater—it has become standard practice to rate field strength as so many microvolts or millivolts per meter. Thus an antenna that has an effective height of one meter and has four microvolts across it is situated in a field strength of four microvolts per meter. The effective height of the antenna is somewhat less than its actual physical height above ground, and in most receiver measurements is assumed as four meters (13 feet). An antenna that has an effective height of 4 meters and a voltage of 10 microvolts across it is immersed in an electric field due to some transmitting station whose strength is 2.5 microvolts per meter.

The greater the field strength at a given point the more volume one can get out of a receiver with a fixed amount of amplification. Similarly the greater the field strength the less receiver amplification is necessary to give out a certain amount of power.

Dr. Alfred N. Goldsmith, in the Proceedings of the I.R.E., October, 1926, has given the following tables which are self-explanatory:

TABLE I

Signal Field Strength	Nature of Service
0.1 millivolt per meter	poor service
1.0 millivolt per meter	fair service
10.0 millivolts per meter	very good service
100.0 millivolts per meter	excellent service
1000.0 millivolts per meter	extremely strong signals

TABLE II

Antenna power	Service Range
5 watts	1 mile
50 watts	3 miles
500 watts	10 miles
5,000 watts	30 miles
50,000 watts	100 miles

Now quoting Lloyd Espenschied in the Bell System Technical Journal, January, 1927, "Fields between 5 and 10 millivolts per meter represent a very desirable operating level, one which is ordinarily free from interference and which may be expected to give reliable year round reception, except for occasional interference from nearby thunder storms.

"From 0.1 to 1.0 millivolt per meter, the results may be said to run from good to fair and even poor at times. Below 0.1 millivolt per meter reception becomes distinctly unreliable and is generally poor in summer. Fields as low as 0.1 millivolt per meter appear to be practically out of the picture as far as reliable high quality entertainment is concerned."

These figures of Goldsmith and Espenschied give us a good idea of what may be expected from stations of certain power at certain distances from the receiver. From these and other data we may assume that a 5000-watt station may be expected to deliver a field of about 10 millivolts per meter at distances up to 20 miles and 1.0 millivolt per meter not over 50 miles. According to the Bureau of Standards paper, "Progress of Radio Measurements," April, 1924, "When WEAF was transmitting with 3 kw. in the antenna its field strength at 10 miles was 32 millivolts per meter. When KDKA had a nominal power of 10 kw. its field at 10 miles was 43 millivolts per meter."

The purpose of the transmitting station is to provide a good lusty signal that will override static and other disturbances; the purpose of the radio-frequency amplifier is to provide the listener with good loud signals from the field strengths which the stations produce.

240. Advantage of high power at transmitting station.—Whatever voltage exists across the antenna, whether noise or desired signal, is amplified by the radio-frequency amplifier; there is therefore a distinct advantage, so far as the receiver is concerned, in using large amounts of power at the transmitting station. The greater the ratio of signal to noise the better will reception be. No matter how great the voltage gain of a radio-frequency amplifier, it cannot bring a weak signal out of the noise and give satisfactory reception. The signal must always be about 40 DB above the noise level in order to provide an entertainment free from a noisy background that is apparent on weak musical passages. Whenever the noise comes up, as on a warm summer day, and the transmitter station power remains constant, reception suffers, and it suffers in a very rapid manner the farther the receiver is removed from the station. The noise about a given receiver is more or less constant under a given set of conditions, whereas the field strength due a transmitter decreases to one-fourth every time the distance is doubled.

If a receiver is situated in a quiet locality, where the noise level made up of stray voltages from street cars, elevators, arc lamps, power leakages from high tension wires to trees, sputtering flat-irons, X-ray machines, etc., is weak, the greater the amount of amplification in the r.-f. amplifier, the greater the distance away a transmitter of a given power can be and still provide an adequate loud speaker signal; and, of course, with this amount of amplification the weaker a station can be at a given distance to provide this loud speaker output. The purpose of the radio-frequency amplifier is the same as of a telescope; it is to decrease the effective distance between the transmitter and the receiver. Unlike the telescope, it cannot be aimed at a particular station but must pick up all the r.-f. voltages not only between it and the desired station but in other directions as well. If the power of the transmitter is increased by 10 DB (ten times the power) the r.-f. amplifier can be made 10 DB less sensitive and thus unwanted signals are automatically reduced 10 DB compared to the desired signal.

241. The task of the radio-frequency amplifier.—The r.-f. amplifier employed in a broadcast frequency receiver may differ decidedly from that used in a receiver serving other purposes or tuned to other frequencies. For example it is possible to make a much more efficient amplifier if it is to work at one frequency instead of at any one of many. A broadcast receiver, for example, must be capable of amplifying at any frequency between 500 and 1500 kc. It must be easily changed from one frequency to another, and its amplification at all frequencies within this band should be uniform. If it selects and amplifies too, its task is much more difficult to perform, as we shall see.

The energy thrust upon the ether from a given broadcasting station is a complex bit of wave motion. If the microphone is idle, what comes from the antenna may be considered as a very narrow band, at say 600 kc., called the **carrier wave.** If a single tone, say 1000 cycles, is put into the microphone, the antenna current has frequencies of not only 600 kc. in it but 599 and 601 as well, and when music is broadcast the frequencies in the antenna may be varying between zero and 5000 cycles above and below the carrier from instant to instant. These frequencies on either side of the carrier are called the **side bands.** The characteristics of the transmitter must be such that each of these audio frequencies is given equal power compared to the others. The resonance curve of the antenna system of the transmitter, then, must not be sharp but must be rather flat or dull as shown in Fig. 181. It must have a rather flat top from 5 kc. below to 5 kc. above its carrier frequency.

If audio frequencies up to 5000 cycles are transmitted, each station requires a channel 10 kc. wide for its transmission, and if there are 1000 kc. available there are 100 channels or places for 100 simultaneous transmissions.

At the listening station, the receiver must be able to pick out any one of these stations, and to receive it without being bothered by others on other channels. This means that a receiver with a good degree of selectivity is one which will receive, transmit, and amplify signals on the band from 595 to 605 kc. but not recognize a signal in the adjacent channels, that is, on the channel extending from 585 to 595 kc. and the channel extending from 605 to 615 kc. In other words, to cope with conditions in the broadcasting band a receiver should have "ten kilocycle selectivity."

242. The ideal response curve of a receiver.—To carry out this double purpose of the r.-f. amplifier the response curve should be a square-topped steep-side curve as in Fig. 181, like the transmitter curve. This is very difficult if not impossible to attain. In practice, the response curve is either so broad that stations on the adjacent band, or even two or three channels away, will be audible during weaker passages of the desired signals, or so selective that the high audio tones are lost, due to what is called "side band cutting." This means simply that the radio-frequency waves corresponding to 600 kc. plus or minus 5000 cycles are cut off in the r.-f. amplifier.

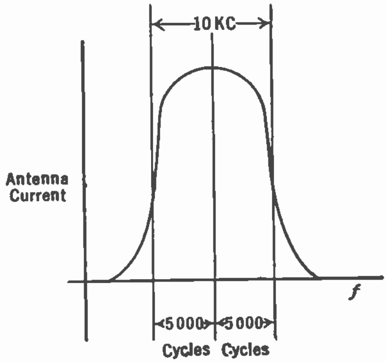


FIG. 181.—A flat-topped steep-sided response curve is the ideal. This curve approaches it.

A receiver which has such a sharp curve that the higher audio tones are discriminated against cannot possibly deliver a high quality loud speaker output even though a flat audio amplifier is used. A receiver that has a flat-top curve usually has too gently sloping sides so it is subject to interference from unwanted signals.

243. Three types of radio-frequency receiving systems.—The majority of receivers for use on broadcast frequencies amplify and select at the same time. They use tuned circuits, and so the receivers are called "tuned radio-frequency sets" or simply, "t.r.f." Because of the steepness of a resonance curve, the overall response of several circuits to frequencies off resonance is diminished, and is a logarithmic function. That is, if two amplifiers deliver ten times as much voltage at resonance as they do at some other frequency the total discrimination in favor of a desired signal is 100 times in a two-stage amplifier, or 10^N if there are N stages.

Another type of receiver, the super-heterodyne or double detector, changes the frequency of the incoming signal to a lower frequency and then amplifies at this frequency. In the frequency-changing process a certain amount of selectivity is developed.

In still another type of receiver the selectivity and the amplification are developed in different circuits. One can either amplify and then select or select and then amplify. A series of tuned circuits is set up which have more or less flat-top and steep-side response curves, which can be tuned so that a band of certain width is cut out of the broadcast frequency spectrum at any desired point. The signals that are passed by this "band selector" are then built up in voltage by an amplifier that has little or no discrimination, that is, it amplifies all signals, no matter of what frequency the same amount, depending upon the selector to pick out the desired signals. Such a selector is called a "band selector" or band pass tuner because it selects or passes a band of frequencies.

Problem 1–13. The response curve of a single tuned circuit in a radio-frequency amplifier is given in Fig. 182. Remembering that the amplification of two stages is the square of one stage, calculate and plot the result of using two such stages. Then calculate and plot the response curve in percentages, using the response at resonance at 100 per cent. Finally, plot this curve in DB using the response at resonance as 0 DB; and, remembering that a station 10 kc. off resonance must be about minus 40 DB in voltage if it is not to be too loud during weak passages of the resonance signal, determine if two stages of such amplification and selection are sufficient. If not, would another stage be sufficient? How many DB does a single stage "put down" a signal 20 kc. off resonance; how many DB down is it after passing through two stages; how many after going through three stages?

Problem 2–13. Suppose a station increases its power from 500 watts to 5000 watts and thereby increases its "service range" (radius) from 10 miles to 30 miles. Suppose the density of population in the area covered by the station's signals is 140 people per square mile. Calculate how many more people can now hear the station and the saving to the community if each listener would have to pay $1.00 each to increase the r.-f. gain of his receiver to get the station properly if it had not increased its power. If it costs the station $35,000 to make this change in power, has it been economical from the standpoint of the community?

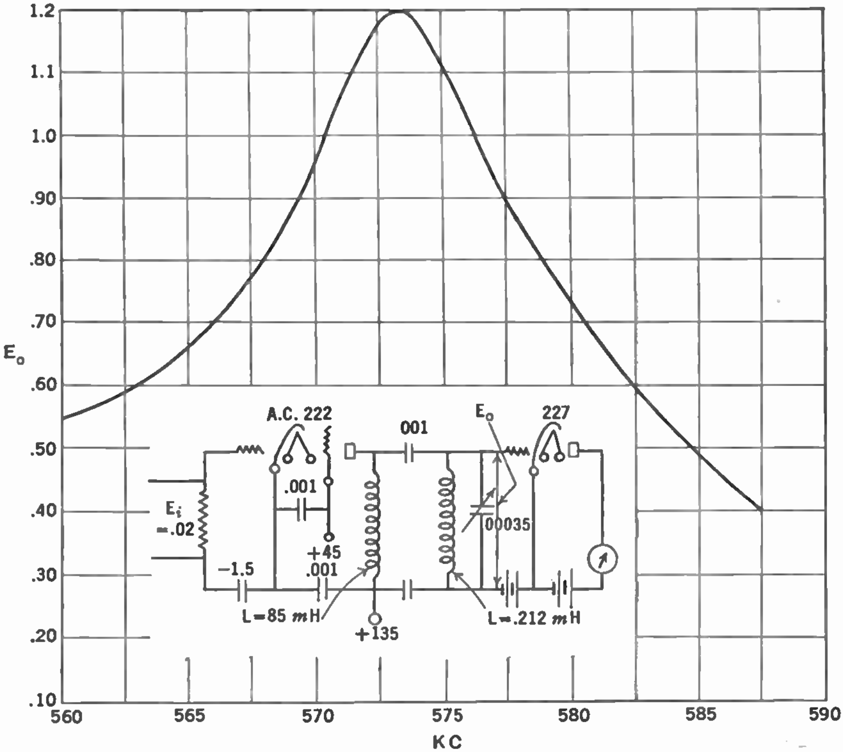


FIG. 182.—Response curve and diagram of connections of single-screen grid stage.

244. Radio-frequency amplifiers in general.—In amplifiers which are to operate at frequencies far above the audio tones with which Chapters XI and XII dealt, we have, in addition to the problems encountered there, several new ones. The difficulty in maintaining amplification with ordinary tubes and circuits at high audio frequencies was mentioned, and the reason—the stray capacities and those due to the tube input circuit—was discussed. These stray capacities in a radio-frequency circuit become much more important, not only for their shunting effect—which is severe at frequencies of the order of one million cycles—but because of other interesting phenomena which will be discussed at this point.

245. Effect of tube input capacity.—In general a voltage amplifier must be one which works from a low impedance into a high impedance load. The problem in all tube amplifying circuits in which high-voltage amplification—at the expense of low-power amplification if necessary— is desired, is to get a high impedance for the tube to work into. Suppose this load impedance is a resistor shunted by the succeeding tube grid-filament path. The effect of the input capacity of this tube upon the load impedance was discussed in Section 198. If the frequency at which the amplifier is to work is multiplied by 100, the shunting effect of the condenser becomes 100 times as great.

Problem 3–13. A tube with a plate resistance of 12,000 ohms and a μ of 8 has a resistor in its plate circuit of 50,000 ohms. The following tube is a UX–240 with an effective μ of 20 and a grid-filament capacity of 4.0 mmfd., a plate-grid capacity of 8.8 mmfd., and a plate-filament capacity of 1.5 mmfd. Other capacities across its ouput circuit bring up the total plate-filament capacity to 6.0 mmfd. What will be the impedance in the plate circuit of the first tube and what will be the voltage gain at 10, 100, 1000 kc.? (Section 178.)

Now it is generally assumed that if an amplifier tube has a sufficiently high grid bias that no grid current flows, the input impedance of the tube is infinitely high and acts as a pure capacity which is given by the expression

$$C_o = C_{gf} + C_{gp}\,(G + 1),$$

where G = the effective amplification;

C_{gp} = the plate-grid capacity;

C_{gf} = the grid-filament capacity.

If this were true at radio frequencies, as is usually true at audio frequencies, we could find a way to get around the shunting effect of the input capacity. But at high frequencies this is not exactly true. The fact that the input impedance is not a pure capacity becomes important. There is resistance as well as capacity in this input circuit, and this resistance may vary from a high positive resistance which absorbs power from the previous tube's output circuit, to a negative resistance which delivers power to the previous circuit.

246. Tuned radio-frequency amplifiers.—The serious shunting effects of the input capacity of the circuit into which a tube works and which make it impossible to build resistance-coupled amplifiers to work at frequencies of the order of 1000 kc. can be avoided by the simple expedient of using this capacity to tune an inductance, or, stated in another way, by balancing out the capacity reactance by means of an inductance. For example in Fig. 183 the effect of the capacity C_o is to so reduce the impedance in the plate circuit that no amplification can result. If, however, we place an inductance across this condenser of such a value that at the desired frequency the coil and condenser form an anti-resonant circuit of very high impedance, the load into which the tube works will be not much less than R and high enough to permit some amplification. Since fairly low resistance coils are easily obtainable, and since the effective resistance of such a tuned circuit is $L^2\omega^2/r$ or L/C_or, a value that may be considerably beyond that of the resistor, we may as well do away with the resistor and use merely the coil and condenser. For purposes of selectivity we may place a variable condenser across C_o and so tune the coil over the entire broadcasting—or other—band.

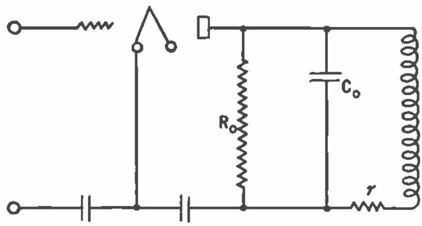


FIG. 183.—Balancing out capacity reactance by means of shunt inductance (L).

Problem 4–13. Suppose an inductance of 200 microhenrys is in the plate circuit of the tube in Problem 3. Its resistance is negligible in comparison to its reactance. Calculate the impedance in the circuit at 1000 kc. and at 1010 kc. and hence the voltage gain. Then assume that the coil has a resistance (r) of 10 ohms, and when tuned by means of a condenser to

1000 kc. calculate the impedance in the circuit at 1000 kc. and at 1010 kc. Calculate the voltage gain of tube and load, and the relative advantage of the tuned circuit in selectivity over the untuned inductance.

The advantages of such a circuit are: first, the effect of the capacity C_o is eliminated; second, the effective resistance in the plate circuit of the tube may be made as high as we desire by making the inductance large and its resistance low (effective values of 100,000 ohms are not difficult to attain); and third, where a resistance amplifier would be absolutely non-selective, this tuned amplifier can be made very selective.

247. Effect of negative input resistance.—Now, such a tuned radio-frequency amplifier works out very nicely theoretically, and practically comes quite close to the final solution, except for one thing. This is the changing input resistance of the tube.

The input impedance of a tube is not a pure capacity. It is a capacity and a resistance. The value of this resistance may be high and positive if the load in the plate circuit of this tube is negative in sign—a capacity load, or negative if the load is inductive and of sufficient value. For example the curves in Fig. 184 (taken from Bureau of Standards Circular No. 351, Effect of Load on Input Impedance of Tubes, by J. M. Miller) show the input resistance of a typical tube at various values of inductance and resistance in the plate circuit. In other words, the minute we put an inductance in the plate circuit of a radio-frequency amplifier, we have done something to the grid circuit of that tube. If (1) the inductance is high enough, we have decreased the input resistance of the tube to a very low value; if (2) the inductance is increased still more, the input resistance becomes negative.

Up to the point when the input resistance becomes negative, it takes power from the circuit to which it is attached, because any r.-f. currents flowing through this resistance must suffer an I^2R loss. But the minute the resistance becomes negative, power is fed into the circuit to which the tube is attached. Now, feeding power into that circuit has the same effect as decreasing the resistance of that circuit by some other means, and when sufficient power is fed into the circuit that all of its resistance has been reduced to zero, radio-frequency currents flow although the input is removed from its original driving source, and the circuit is said to oscillate. Direct-current power from the batteries is used up in producing and maintaining radio-frequency power in the coils and condensers. The circuit is useless as an amplifier.

We come then to this impasse, that, to get any amplification out of a tube at radio frequencies, we must put an inductance in its plate circuit and tune that inductance with a condenser. Putting

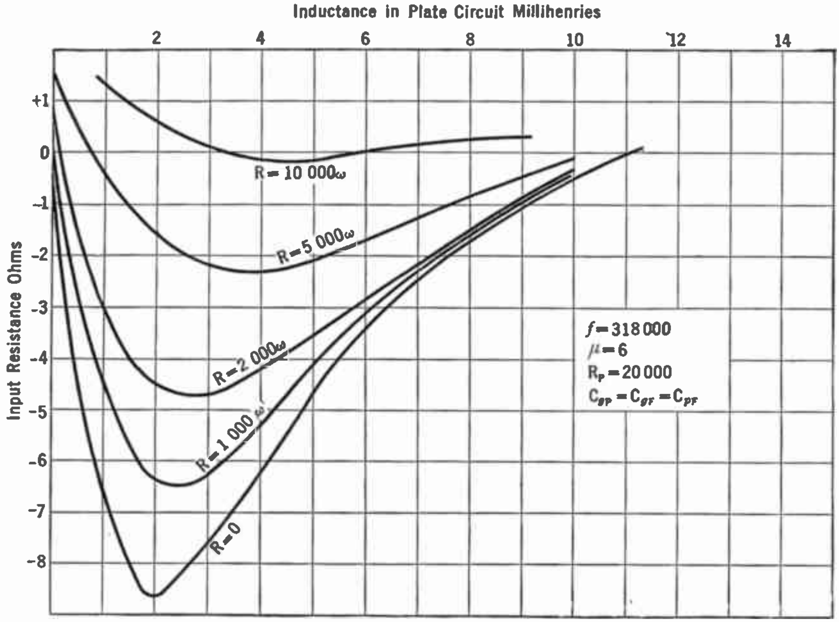


FIG. 184.—Dependence of input resistance upon inductive load.

the inductance in the plate circuit reduces the input resistance of the tube, and when the inductance is tuned to resonance, the circuit is in a highly critical condition. Any increase in inductance, or decrease in capacity—which amounts to the same thing—is liable to make the whole system oscillate. Any inductance in the plate circuit reduces the resistance in the grid circuit and results in a reduction in the effective resistance losses in the circuit out of which it works. So any resonant circuit that may be present—an antenna for instance—becomes very sharply tuned, and the higher audio frequencies are completely lost. The circuit is said to be regenerating. Regeneration is merely a minor case of oscillation.

For the moment let us forget this trouble from regeneration and oscillation with the remark that it is caused by the inter-electrode capacity of the tube, and is of sufficient magnitude to have prevented efficient r.-f. amplifiers from becoming generally used for a long time after the need for such equipment was felt. Let us look into the tuned radio-frequency amplifier, just as though we never heard of oscillation or regeneration, and see what engineering we can bring to bear on the problem of getting the most amplification and the best fidelity with the apparatus at hand.

248. Engineering the tuned radio-frequency amplifier.—The inductance and capacity required for resonance at any point in the broadcast frequency band (550 to 1500 kc.) may be calculated easily. These values are more or less fixed by the sizes of condensers generally available. Let us suppose their values are such that with the resistance of the coil taken into consideration they produce an effective resistance at resonance L/Cr (an anti-resonant circuit) of 100,000 ohms. In the plate circuit of a 12,000-ohm tube this load should give considerable amplification except for the fact that bridging a resistance of 12,000 ohms across such a coil-condenser combination would have the same result as adding considerable resistance in series with the coil, and therefore the effective resistance into which the tube works will decrease at an alarming rate.

For example, if the effective resistance of a coil condenser combination is 100,000 ohms and is shunted by a 12,000-ohm tube, the equivalent impedance is now reduced to 10,700 ohms which represents the same change produced in the selectivity of the anti-resonant circuit as if its resistance had been increased by something over nine times. Of course this would give a very poor degree of selectivity, and the voltage amplification would not be as high as desired.

If, however, we use a transformer with a step-up ratio from the plate of one tube to the next grid circuit, the plate resistance is stepped up by the turns ratio squared and is then placed upon the tuned circuit. If, for example, the turns ratio between secondary and primary is 4, the effective resistance placed across the tuned circuit would be $12{,}000 \times 4^2 = 193{,}000$ and so the resistance of this tuned circuit would be increased only by a ratio of 10 to 6.1. Furthermore, there is a voltage step-up in the transformer, therefore some voltage gain may be secured by its use. Of course this transformer need have only one winding, the input coil to the following tube being tapped as in Fig. 185 for the plate inductance of the previous tube, an auto-transformer, in fact.

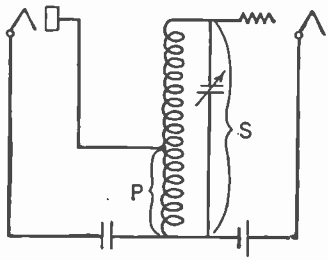


FIG. 185.—Proper selection of the tap will provide maximum voltage amplification.

In this case the transformer may be looked at as a kind of selectivity adjuster, since one can adjust the selectivity by its use.

Let us look at the problem in another way. A transformer with tuned secondary will give maximum power in the secondary load and maximum voltage across the secondary when the resistance across secondary and primary are related by the proper turns ratio. If, then, the load across the secondary is the effective resistance of the secondary when tuned to resonance, and the resistance across the primary is the plate resistance R_p of the preceding tube, the proper turns ratio can be found by the usual means, namely,

$$\frac{Z_s}{Z_p} = N^2 = \frac{L^2\omega^2}{rR_p} = \frac{L}{C_rR_p},$$

whence

$$N = \frac{L\omega}{\sqrt{rR_p}},$$

and when this turns ratio is used the voltage gain of tube and transformer is

$$G = \frac{\mu}{2} \times \frac{L\omega}{\sqrt{rR_p}}.$$

This expression involving the turns ratio is not the number of turns on the secondary divided by the number of turns on the primary because in an air core transformer of this type it is not possible to obtain 100 per cent coupling, but for the moment let us not bother about this problem. We shall return to it later. The actual turns ratio is somewhat greater than N, and can be determined by experiment.

249. Gain due the tube and gain due the coil.—There are two parts to the above expression for the voltage gain of tube and transformer. Part is due the tube and part is due the transformer. That is, we may divide up this expression into two parts.,

$$G = \tfrac{1}{2}\frac{\mu}{\sqrt{R_p}} \times \frac{L\omega}{\sqrt{r}},$$

in which the first part shows that the gain is proportional to one-half the μ of the tube divided by the square root of its plate resistance and the second part shows that the gain is proportional to the inductive reactance of the coil divided by the square root of its high-frequency resistance. From such an expression we may learn several things.

In the first place G is the maximum possible voltage gain that can be obtained from a given tube working into a given resistance and this is obtained only when the turns ratio N of the transformer is properly adjusted. For a certain tube, the expression $\frac{\mu}{\sqrt{R_p}}$ is a constant and is related to the mutual conductance although once we have determined its value we can multiply it into the corresponding values for the voltage gain due the transformer and we then have the maximum voltage gain. The figure of merit for the transformer $(L\omega/\sqrt{r})$ is not constant over the broadcast frequency band as the curve in Fig. 186 shows, and from it we learn at once that the overall gain, G, of tube and transformer will not be equal at all frequencies unless the overall gain is reduced. This is because the maximum gain is being secured at the low frequencies, and there is but one way to flatten the curve, that is, to decrease the high-frequency gain.

We are now in a position to perform a very interesting experiment, one that requires neither laboratory nor apparatus. We need only a pencil, some paper, a slide rule, some values of the factors that enter into the expression for the maximum voltage amplification, G.

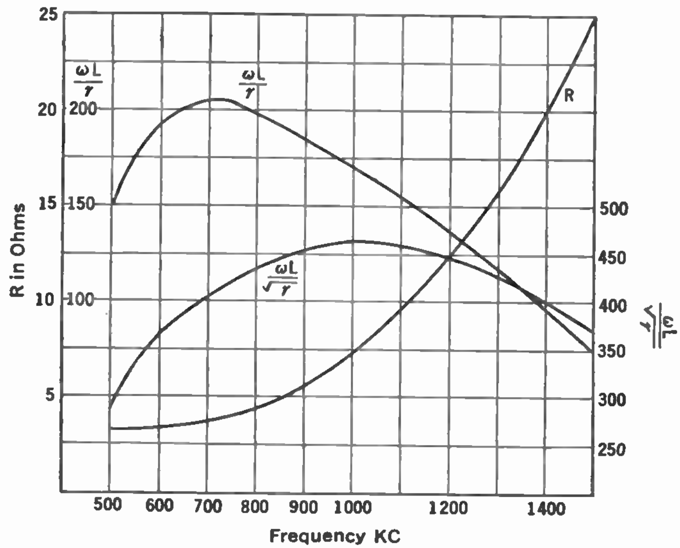


FIG. 186.—How resistance and figure of merit "Q" $\left(\frac{\omega L}{r}\right)$ of a coil vary with frequency.

Experiment 1–13. A coil has an inductance of 168 microhenrys, and a high-frequency resistance, r, of 4 ohms at 700 kc., 6 ohms at 1100 kc., and 9 ohms at 1500 kc. Plot this resistance against frequency. Calculate the figure of merit $\left(\frac{L\omega}{\sqrt{r}}\right)$ for the coil and plot against frequency. Assume it to be used out of a tube whose plate resistance is 12,000 ohms and whose μ is 8. Calculate the proper turns ratio for maximum voltage amplification at the above frequencies and what the amplification is, that is, calculate and plot $N = \frac{L\omega}{\sqrt{R_p r}}$ and $G = \frac{1}{2}\mu \times N$ against frequency, assuming that the proper turns ratio is used at each frequency.

Then calculate N and the voltage amplification at 1000 kc. of such a coil and a 199 tube with a plate resistance of 16,000 ohms and μ of 6.6, and then when a 240 type tube is used. It has a plate resistance of 150,000 ohms and a μ of 30.

Problem 5–13. The effective resistance of a coil-condenser combination is 100,000 ohms when the resistance of the coil is 10 ohms. That is, $L/C\,r =$ 100,000 ohms, where r is the series resistance. Calculate what the equivalent resistance of such a circuit is when shunted by 10,000 ohms. (Two resistances in parallel have a resistance equivalent to their product divided by their sum.) Then assuming that this value is the effective resistance of another tuned circuit having the same L and C but a different series resistance, calculate what the value of r is.

Problem 6–13. A tube of 5000 ohms (UX–112A) is to be used as an r.-f. amplifier and to be worked into a tuned circuit whose effective resistance is 120,000 ohms. What is the proper turns ratio for maximum voltage amplification and what is the amplification? Remembering that a resistance across a primary of a transformer is equivalent to another resistance across the secondary stepped up by the square of the turns ratio of this transformer, what is the equivalent resistance that is placed across the tuned circuit by this transformer? What happens to the effective resistance $L/C\,r$ of this circuit?

Problem 7–13. A voltage gain of 10 is desired. The plate resistance of the tube is 12,000 ohms, its μ is 15, the inductance of the coil is 186 microhenrys, and the capacity is 0.0001 mfd. What is the maximum resistance the coil can have?

250. Effect of coupling.—The foregoing argument on maximum possible amplification of tube and its accompanying transformer has been based on the assumption that the coupling between primary and secondary was adjusted to the proper value at each frequency. Actually, such is seldom or never the case, and even if it were it is doubtful if receiver designers would so choose the coupling that maximum amplification would result owing to the decrease in selectivity of the circuits under these conditions.

In general the voltage amplification of a tube and transformer when the secondary is tuned may be expressed as

$$G = \mu \frac{\omega^2 M L_2}{R_p R_s + \omega^2 M^2},$$

which involves not only the resistance of the apparatus (R_p and R_s) on the two sides of the transformer but the coupling M in the transformer itself. If we go into the laboratory and measure the voltage across the secondary with a constant input voltage to the tube but with various degrees of coupling we shall get a curve similar to that in Fig. 187 (A. I. E. E. Journal, May, 1928, R. S. Glasgow, Tuned Radio-Frequency Amplifiers), which is the experimental proof of our statement that the coupling must be adjusted for maximum voltage transfer.

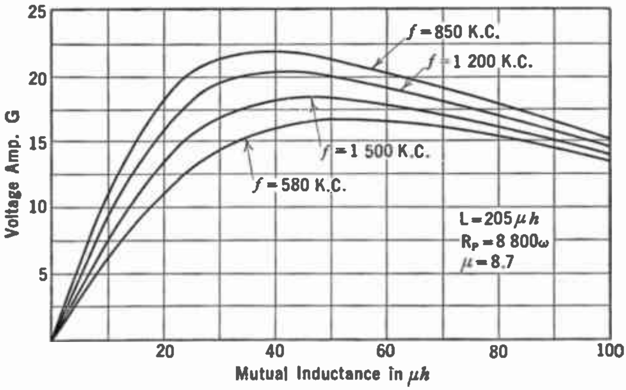


FIG. 187.—Relation between coupling and amplification.

251. Effect on secondary resistance, of close coupling.—The increase in resistance—and consequent decrease of selectivity—of the secondary circuit may be calculated from the expression

$$r = \frac{M^2\omega^2}{R_p},$$

which states that the resistance introduced across the secondary by the transformer is equal to the square of the mutual reactance divided by the resistance in the primary, in this case the plate resistance of the tube. This resistance introduced across the secondary increases as the frequency and the mutual inductance squared and is inversely proportional to the plate resistance of the tube out of which the transformer works. This means simply that the greater the impedance of this tube, the less will the selectivity be decreased with a given turns ratio, and the reason for such an inverse function is simply that a larger resistance shunted across the tuned circuit will introduce less resistance in series with that circuit than will a smaller resistance across the circuit. No matter what the plate resistance, if M is adjusted for maximum possible voltage amplification the selectivity of the secondary circuit will be cut in half, because this selectivity is a function of the series resistance of the secondary which is doubled when the turns ratio is such that G is a maximum. Now the coupling between primary and secondary is controlled not only by the physical proximity of the two windings, but upon the number of turns in the primary, if the secondary turns are held constant. Therefore, decreasing the primary turns will increase the selectivity and decrease the amount of voltage amplification. Mathematical analysis of the problem will show that decreasing the turns in the primary from the number required for optimum voltage transfer to zero, only increases the selectivity by a factor of two. This means simply that when the number of turns in the primary is zero, none of the plate resistance of the tube is transferred to the secondary circuit, and, of course, then the selectivity of the secondary is its selectivity when standing alone. No voltage is transferred under this condition, and so such selectivity for a single stage is never attained.

There is another variable factor in this transformer, this is the ratio of L to C. We have already discussed the voltage gain and selectivity as controlled by the secondary resistance and the turns ratio and the plate resistance of the previous tube. Calling upon either experimental proof or mathematical analysis, we can show that the greater the inductance of the secondary, other factors being maintained, the greater will be the selectivity of the system, and that when the secondary is adjusted to give the maximum amplification, given by

$$R_p R_s = \omega^2 L^2$$

(where $\omega = 2\pi \times$ resonant frequency) the selectivity will depend upon the ratio of L to R_s (secondary resistance) only and that if the circuit is adjusted for the greatest amplification for a desired signal it will also give the smallest amplification to an unwanted signal (K. W. Jarvis, Proc. I. R. E., May, 1927). Other curves showing the influence of coupling, etc., on selectivity and amplification are shown in Figs. 188 and 189.

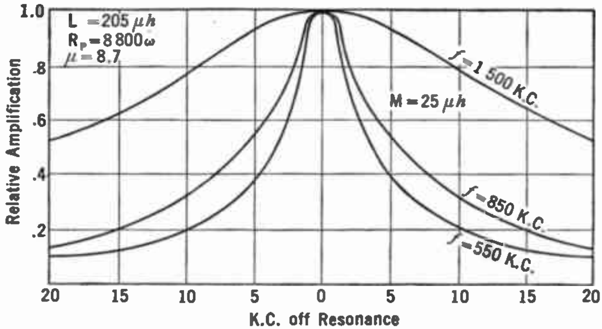


Fig. 188.—Curves showing how selectivity of tuned r.-f. circuit depends upon frequency.

252. Selectivity.—So far we have treated the selectivity problem in a qualitative way only. We have not said anything about how much selectivity we needed or desired, or how much we could get. We stated that increasing the coupling between the primary and secondary circuits (decreasing N) of our tuned transformer increased the resistance in the secondary circuit and thereby decreased the selectivity of that circuit, and that at the coupling for maximum voltage gain the selectivity was halved. What does this mean? How much selectivity is needed to prevent cross-talk between stations 10 kc. apart? How much selectivity

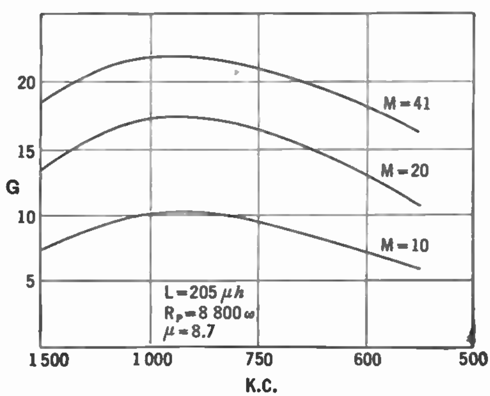


Fig. 189.—Relation between mutual inductance and gain in an r.-f. amplifier.

can be secured? What are the coil characteristics to provide such selectivity? How much selectivity can be tolerated before side band cutting becomes audible to the ear? These are questions that assail every receiving set engineer.

In Chapter VII we discussed the simple series resonant circuit, and stated that the steepness of its response curve at resonance depended upon the resistance in that circuit. The greater the resistance, the duller the curve, and the less difference in voltage, or current, between the resonant frequency and frequencies off resonance by say 10 kc. In fact the width of the resonance curve is a direct measure of the resistance in the circuit. Consider such resonance curves as that in Fig. 188. If f_1 and f_2 are two frequencies on either side of the resonant frequency, f_r, such that the current, or voltage, at these frequencies is 0.707 of the value of voltage, or current, at resonance, then the following formula is true:

$$\frac{L\omega}{r} = \frac{f_r}{f_2 - f_1}.$$

Here again we run into an expression involving the inductive reactance and the ohmic resistance of the coil. It states that knowing the value of $L\omega/r$ of the coil, we can tell at once how wide the resonance band is going to be at a point where the current, or voltage, is 0.707 of its maximum value. (This amounts to a 3 DB loss in voltge in a single circuit.) How is this useful in our present problem?

The tuned transformer used in t.r.f. sets, or neutrodynes, or in any system in which the secondary of a transformer is tuned, may be considered as a simple series circuit provided we choose the constants of that series circuit correctly. The resistance of that circuit will be its series resistance, r, usually consisting of the high-frequency resistance of the coil alone, plus the resistance " reflected " into that circuit by the transformer. This resistance considered as shunted across the tuned secondary is the plate resistance of the tube stepped up by the square of the effective turns ratio of the transformer, just as in any transformer case.

Now any resistance shunted across the tuned circuit is equivalent to a smaller resistance in series with the circuit, and such a resistance is the controlling factor in determining the width of the resonance curve. And since selectivity is but a term describing the width of this resonance curve, we have in our hands all the necessary facts regarding the voltage amplification and the selectivity of such circuits.

For example, at the coupling between the primary and secondary for maximum voltage amplification the effective turns ratio is given by

$$N^2 = \frac{Z_s}{Z_p} = \frac{L^2\omega^2}{rR_p},$$

which means that the secondary of the coil will be shunted by a resistance equal to the plate resistance of the previous tube multiplied by the turns ratio squared, and this numerically will be equal to the effective resistance of the tuned secondary, $L^2\omega^2/r$. Now the secondary effective resistance, being shunted by another resistance equal to it numerically, becomes half its former value (two equal resistances in parallel have a resultant resistance of one-half of one of them). Such a decrease in effective resistance can also be produced in one other way—by increasing the resistance of the coil to twice its normal value. And what effect has doubling the coil resistance upon selectivity? Clearly it halves it, because selectivity may be thought of as proportional to $L\omega/r$ and doubling r halves this factor.

The following example may fix the whole problem in one's mind.

Example 1–13. Consider a coil whose inductance is 200 microhenrys, and whose resistance r at 1000 kc. is 10 ohms. This coil is to be tuned and fitted with a primary to work out of a tube whose plate resistance is 12,000 ohms and whose μ is 8. What is the proper turns ratio for maximum voltage amplification? What is the voltage amplification? What is the width of the frequency band with and without the tube connected across the primary?

Effective resistance of coil-condenser alone

$$= \frac{L^2\omega^2}{r} = \frac{(200 \times 10^{-6})^2\,(10^6 \times 6.28)^2}{10}$$

$$= 158{,}000 \text{ ohms}$$

Width of frequency band when $I = .707$ maximum value

$$= f_2 - f_1 = \frac{f_r r}{L\omega} = \frac{r}{2\pi L}$$

$$= \frac{10^6 \times 10}{200 \times 10^{-6} \times 6.28 \times 10^6}$$

$$= 8000 \text{ cycles.}$$

Turns ratio for maximum voltage amplification

$$= \sqrt{\frac{Z_s}{Z_p}} = \sqrt{\frac{158{,}000}{12{,}000}} = 3.6.$$

Voltage gain

$$G = \frac{\mu L\omega}{2\sqrt{r\ R_p}} = \frac{8 \times 200 \times 10^{-6} \times 6.28 \times 10^6}{2\sqrt{12{,}000}\ \sqrt{10}}$$

$$= 14.5 \text{ times.}$$

Resistance reflected from primary to secondary

$$= Z_p \times N^2$$
$$= 12{,}000 \times 13 = 158{,}000.$$

New effective resistance of secondary circuit

$$= \frac{158{,}000 \times 158{,}000}{158{,}000 + 158{,}000} = 79{,}000 \text{ ohms} = \frac{L^2\omega^2}{R_1}.$$

New effective series resistance in secondary

$$= R_1 = \frac{L^2\omega^2}{79{,}000} = \frac{158{,}000 \times 10}{79{,}000} = 20.$$

Width of frequency band where $I = .707$ maximum value

$$= f_2 - f_1 = \frac{f_r R_1}{L\omega} = \frac{10^6 \times 20}{200 \times 10^{-6} \times 6.28 \times 10^6}$$

$$= 16{,}000 \text{ cycles.}$$

This indicates that a voltage gain of 14.5 would be obtained with such a coil-condenser combination and tube at a frequency of 1000 kc. and that at a frequency 8000 cycles either above or below resonance, the current in the secondary circuit, or the voltage across it, would be 0.707 of its value at exact resonance. This voltage ratio corresponds to a loss of 3 DB, which is not very great. The selectivity of the transformer and tube, then, is not very great, certainly not great enough to provide much discrimination between a station on 1000 kc. and another at 1010 kc. According to the data of Espenshied (Problem 16–12) we need to be "down" about 40 DB at the frequency of an unwanted station so that its signals will not interfere.

253. Summary of radio-frequency amplifier phenomena.—A discussion of voltage amplification and selectivity and of the constant compromise that must be made between them will be found in Professor Hazeltine's Patent No. 1,648,808.

The gist of this excellent discussion follows. If the physical coupling between primary and secondary is close, the turns ratio between secondary and primary will be assumed equal to N. We shall assume that there is no appreciable capacity across the primary and that the circuit does not tend to regenerate. It has been properly neutralized.

At resonance at a given frequency the voltage amplification is given by

$$G = \frac{N\mu}{1 + N^2 \dfrac{g}{g_r}},$$

where N = turns ratio;

μ = amplification factor or tube = 8;

$$g = \frac{r}{L^2\omega^2} = \frac{Cr}{L} = .01667 \text{ millimho};$$

$$g_r = \frac{1}{R_p} = 0.1333 \text{ millimho},$$

whence R_p = 7500 ohms

$$\frac{L^2\omega^2}{r} = 60{,}000 \text{ ohms}.$$

Using this formula and the special data given on it for a special set of conditions, the curves in Fig. 190 were plotted, which tell us a great deal regarding sensitivity, and selectivity as a function of the turns ratio between primary and secondary. In Fig. 190 we have indicated the several values of N, which is always equal to the total number of turns divided by the number used as a primary.

With $N = 1$, the voltage amplification at resonance is equal to 16.1 DB (a voltage amplification of about 8). Now the horizontal axis represents percentages off resonance. That is, if the resonant frequency is 1000 kc. the point marked " 0.10 " is actually 100 kc.

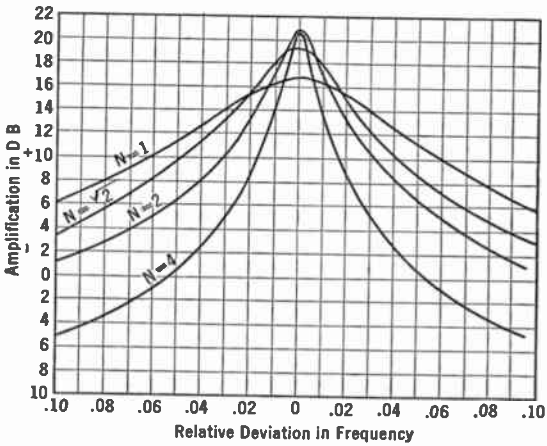


Fig. 190.

(1000 × 0.1) off resonance. If the resonance frequency is 600 kc. this point will be 60 kc. above or below resonance. At this point, with unity turns ratio, $N = 1$, between primary and secondary, the amplification has only decreased to 6.1 DB, a loss of only 10 DB, 100 kc. off resonance. This is poor selectivity.

When N is increased to $\sqrt{2}$ the amplification has increased and so has the selectivity. The amplification is now 17.5 DB and at 100 kc. (for a 1000 kc. resonant frequency) the amplification is only 3.4 DB.

The amplification soon begins to fall off with increase in turns ratio (decrease in primary turns) but fortunately the selectivity increases, and so there is a point at which the best compromise between selectivity and sensitivity can be reached.

The fact that the selectivity changes at each frequency is clearly indicated by these figures. At 1500 kc. and a turns ratio of 4, there is a loss of 25.5 DB at 150 kc. off resonance, but at 550 kc. the same loss occurs at only 55 kc. off resonance. The response curve at this frequency would be almost 3 times as sharp as that at 1500 kc.

The curves show conclusively the fact that there is a certain turns ratio which produces the greatest amount of amplification, and that the selectivity increases as the turns ratio is increased. The best value, according to this discussion, for N is about 2.85 at which the selectivity-amplification ratio is the best. Further increases in the turns ratio produce too great a drop in amplification to be economical. Selectivity must be gained in some other way. This value of N depends upon coil and tube constants.

Now let us look at these curves with the problem of fidelity in mind. The response at 5000 cycles off resonance must not be too much decreased over that at resonance. Thus at 1500 kc. at a point 0.5 per cent (0.005) off resonance or 7.5 kc. the drop in amplification with $N = 1$ is only 0.1 DB. At the most selective frequency, 550 kc., the loss at 5.5 kc. is only 0.1 DB.

Now the designer of the radio-frequency amplifier has several factors under his control in addition to the turns ratio. One of these is the resistance of the coil he uses; another is its inductance. Decreasing the resistance increases the resonant amplification but does little to the amplification 10 per cent off resonance. This amounts to an increase in selectivity. The turns ratio for maximum amplification at decreased resistance must be increased.

If the impairment of fidelity occasioned by using better coils must be overcome, a change in turns ratio to give equal fidelity still gives some increase in sensitivity but with the same selectivity and fidelity, of course. The turns ratio, N, would be decreased in this case. The gain in sensitivity, however, would probably not be worth the effort because of the greater bulk of the coil necessary to get a much lower resistance. According to Hazeltine, at the lower broadcast frequencies (600 kc.) fidelity begins to limit the extent which one can go in the desire for low loss coils. Coils of greater dimension than 3 inches cannot be used unless fidelity is permitted to suffer. Since it is rare indeed that a single radio-frequency amplifier is used, and has become standard practice to use several stages, each of which in itself has rather poor selectivity, the use of coils of small diameter is almost universal. There are other advantages as we shall see later.

There is one other variable; the designer can change the ratio of inductance to capacity. He can use a large inductance and a small capacity or a small inductance and a large capacity within the limitation that the same frequency range will be covered. Doubling the inductance, halving the maximum capacity, and keeping the high-frequency resistance of the circuit constant—a difficult if not impossible requirement, and using the proper turns ratio will increase the amplification at resonance without decreasing the selectivity or fidelity. For example increasing the ordinates of all the curves in Fig. 190 by 3 DB will give the result of doubling the inductance, etc.

254. Selectivity to signals far off resonance.—The curves in Fig. 190 show that to signals far from resonance the amplification is a negative quantity. This means simply that there is a loss at these frequencies, and that at the end of several stages signals far from resonance will be weaker than if only the final stage were used. This is one argument for careful shielding. The direct pick-up by the detector circuit of an unshielded set may cause a greater signal from an unwanted station than would be heard if the preceding and detector input were carefully shielded. There is then no direct pick-up, and whatever gets to the detector input must come through the antenna-ground channel.

The amplification of frequencies 10 per cent off resonance is practically independent of the ratio of resistance to reactance of the transformer, and so variations of coil resistance at various frequencies within the band over which the receiver will be tuned will not make much difference to signals far from resonance.

255. Use of several stages of radio-frequency amplification.—The preceding summation of the Hazeltine paper has regard to a single stage only. Such a single stage will not give enough amplification except over medium distances, and not enough selectivity to cope with the multiplicity of stations in the United States. It becomes necessary to use two or more stages. In this case, the voltage gain of the entire amplifier may be obtained by multiplying the ordinates of a single response curve by the number of identical stages employed. The same result will be secured by adding the DB gain or loss at each point on the response curve of a single stage. Increasing the number of stages increases the amplification at resonance, increases the selectivity and impairs the fidelity unless the turns ratio between stages is varied so that constant fidelity results. The data in the table below are from Hazeltine's discussion in the Proceedings of the I. R. E. which gives the significant statement, " with constant fidelity the selectivity is increased as the number of stages, whereas with a fixed number of stages the selectivity can be increased only at the expense of fidelity."

Number of Stages, *n*	With Constant Turns Ratio			With Constant Fidelity		
	Turns Ratio, *N*	Amplification per Stage, DB	Total Amplification, DB	Turns Ratio, *N*	Amplification per Stage, DB	Total Amplification, DB
1	4	24.1	24.1	....	....	....
2	4	24.1	48.2	6.21	23.3	46.5
3	4	24.1	72.2	4.67	24.0	71.9
4	4	24.1	96.2	4.00	24.1	96.3
8	4	24.1	192.6	2.96	23.7	189.6
16	4	24.1	383.3	2.31	22.8	365.6
....	4	24.1	....	....	....	....

256. Coil factors.—So far as the coil in our radio receivers is concerned selectivity is proportional to $\frac{L\omega}{r}$, the effective turns ratio for maximum voltage gain $N = \frac{L\omega}{\sqrt{rR_p}}$, and the maximum possible voltage amplification at any frequency $G = \frac{\mu}{2} \times \frac{L\omega}{\sqrt{r}} \times \frac{1}{\sqrt{R_p}}$.

The data in the following table give the width of band passed, maximum voltage amplification, etc., at three frequencies in the broadcast band using a tube whose μ is 8, and plate resistance is 12,000 ohms, with a coil of 200 μh. In each case the proper turns ratio is given and the maximum voltage amplification, G, is calculated for the case in which this turns ratio is used.

Out of such a table may be gleaned several interesting facts. In the first place the amplification is not constant over the frequency band. In fact in a frequency band that varies from 500 to 1500 kc. (3 to 1 change in frequency) G varies about 2 to 1, and the turns ratio to produce this gain varies in the same ratio, and the width of the frequency band at the 0.707 voltage point differs at each radio frequency.

Frequency	r of Coil	$\frac{L\omega}{r}$	$R_{\text{eff}} = \frac{L^2\omega^2}{r}$	Width of Band, Coil Alone	N	G	Width of Band
500 kc.	6	104	66,600	4,770	2.4	7.3	9,540 cycles
1000 kc.	10	125.6	158,000	7,950	3.6	14.5	16,000 cycles
1500 kc.	15	125.6	188,400	12,000	4.0	16.0	24,000 cycles

257. Turns ratio into detector tube.—A grid leak and condenser detector has a low input resistance because of the flow of grid current. This resistance is of the order of 60,000 ohms into which the previous r.-f. amplifier must work. The turns ratio, for maximum voltage amplification, of the transformer coupling the detector and the previous tube must be somewhat lower than between two r.-f. amplifier tubes. This type of detector, however, is notoriously broad in tuning because of this low input resistance, and for this reason the turns ratio as used in commercial practice is kept fairly large so that the tuning of the detector does not differ appreciably from that of the other tuned circuits.

258. Regeneration and oscillation in r.-f. amplifiers.—All of the discussion up to this point assumes that the tubes and transformers operated in a stable manner, repeating into the plate circuit what appears in the grid circuit in amplified form, and not repeating back to the grid circuit any of this amplified voltage. Practically, such conditions do not hold. Unless precautions are taken, the circuit oscillates long before the proper inductance has been added to the plate circuit to provide a reasonable amount of amplification.

There are two reasons for this unwanted oscillation. One lies in the unintentional couplings provided between output and input circuit, for instance through mutual inductance between the coils, through capacities which connect the two circuits, and through other couplings. The other source of coupling is also unintentional but, unlike those mentioned above, cannot be eliminated. This second coupling is that existing within the tube, and is due the capacity between the plate and the grid. So long as the plate and grid are at different potentials there will be a capacity current, and since the plate is part of the output circuit, and the grid is part of the input circuit, what takes place in one circuit has some effect on what is taking place in the other circuit.

Let us look at Fig. 191 and assume that there is an amplification in voltage of 10 in the tube, that is, whatever voltage, E_i, is placed across the input appears as 10 times this value in the output. The voltage is applied to the input through the mutual inductance between the primary, *P*, and secondary, *S*, of the transformer. Whatever a.-c. current flows in the plate circuit must also go through the coil, *T*, commonly called a "tickler." If this coil is coupled to *S* in the proper manner, it will induce a voltage in the input coil *S* in such a direction that it will be in phase with the voltage induced there from *P*. Suppose the voltage due *P* is 1.0 volt and that the voltage on *S* due to *T* is one-half volt. We now

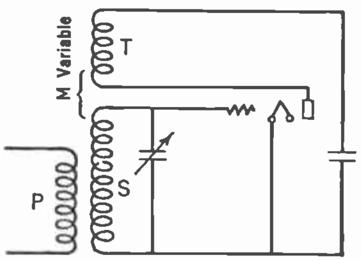


FIG. 191.—A simple regenerative circuit.

have not 1 volt on the grid of the tube but 1.5 volts. This is what is known as regeneration; part of the output voltage is fed back to the input and *in phase*. When the feed-back voltage is of the correct magnitude and phase, we may remove the input voltage due the primary, *P*, and a.-c. currents will still flow because whatever came from *P* originally has been amplified in the tube and fed back to the grid where it is amplified again, and again returns to the input. In other words the tube oscillates; it supplies enough energy from the B battery to wipe out all the losses in power in the circuit.

Let us look at the phenomenon of regeneration in another way. Suppose the input circuit to the tube is tuned. The current in the tuned circuit is controlled by the resistance in that circuit—provided a constant voltage is impressed from *P*. If, now, we decrease the resistance in the circuit the current increases, and the voltage across the circuit (and hence on the grid) increases.

Now suppose the voltage across the input is increased by means of the tickler coil, *T*. This produces exactly the same result as if the resistance in the tuned circuit were decreased. We may express what has happened by stating that feed-back, if in proper phase and magnitude, may introduce a *negative* resistance into the tuned circuit. This negative resistance added to the already existent positive resistance decreases the total resistance there. When the tube feeds back sufficient negative resistance so that the entire resistance losses in this circuit are wiped out, the system maintains itself in a state of continuous oscillation requiring no additional a.-c. energy from without, and capable of supplying considerable a.-c. power to some external circuit coupled to it.

Such a feed-back of voltage from the plate to the grid circuit may take place through desired coupling—as in case of the tickler feed-back—or through unwanted coupling, as mentioned above. The grid-plate capacity is the most prolific source of trouble from regeneration, because the voltage fed back from this small inter-element capacity may be of the proper phase and magnitude to cause not only regeneration but oscillation as well.

Section 245 mentioned the fact that the input impedance of a vacuum tube is not a pure capacity, but that it may be a capacity plus a resistance which may be either positive or negative depending upon the load in the plate circuit. If the load is a positive reactance, an inductance, the input resistance of the tube may be negative, and so the voltage fed back there from the plate circuit through the grid-plate capacity will be in phase with the voltage already appearing there. Regeneration takes place. If the resistance of the input circuit is sufficiently negative the circuit may oscillate.

If the load in the plate circuit is a negative reactance, a capacity, the input resistance of the tube will be positive, and will shunt the input circuit. If this circuit is a coil-condenser combination tuned to resonance with some incoming voltage, the positive resistance of the grid-filament circuit of the tube will be placed across this tuned circuit and of course will decrease its selectivity.

The input impedance of a tube, then, depends upon the plate load. Any change occurring in the plate circuit is repeated back to the input grid circuit through unwanted couplings, usually through the grid-plate capacity, and may cause either regeneration due to an inductance load or degeneration due to a capacity load, which produces a positive input resistance.

If the load in the plate circuit is resistive or capacitive the tube and circuit cannot regenerate or oscillate. Signals may even be weaker. In Fig. 192 if the plate circuit is exactly tuned to resonance with the frequency of the signals coming from the input circuit, the plate load is resistive—the impedance of an anti-resonant circuit at resonance is resistance only—and so the circuit will not oscillate, a fact that is often overlooked. If the condenser capacity is greater than that required for resonance, the load in the plate circuit is essentially capacity and the circuit cannot oscillate. If, however, the condenser is reduced, so that the circuit begins to act like an inductance, the circuit begins to regenerate and finally oscillations may begin. If the plate circuit capacity remains fixed and the

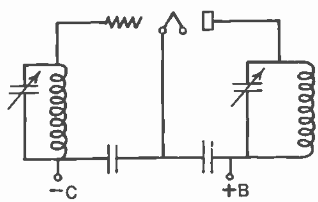


FIG. 192.—Tuned plate-tuned grid circuit.

frequency of the input signals is varied, a frequency will be reached which makes the plate circuit resonant. For frequencies above this critical value the plate circuit is capacitive, and no regeneration takes place. For frequencies lower than this critical frequency the load is positive (inductive) and regeneration begins.

259. Losses.—We are faced with the predicament of having to use inductance in the plate circuit in order to transfer energy from one tube to another and of having to cope with unwanted regeneration or oscillation due to this positive reactive plate load. What can be done about it?

There are several ways in which receiver designers have tried to solve the problem. The negative resistance introduced into the

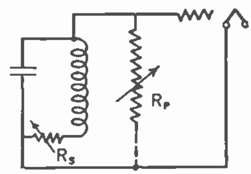


Fig. 193.—Series (R_s) and parallel (R_p) losses added to prevent oscillation.

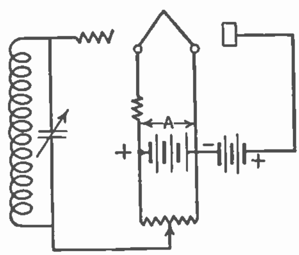


Fig. 194.—Potentiometer method of controlling oscillations.

grid circuit by the plate-grid capacity may be reduced by adding resistance to this circuit. This resistance may be added in series with the tuned circuit, as R_s Fig. 193, or across it, as R_p. Oscillation can take place only when the total losses in this tuned circuit are wiped out by the feed-back voltage, and so, having the losses under control of the operator, the circuit can be maintained in a stable condition at all times.

Another method is the potentiometer method, as in Fig. 194, where a potentiometer is across the A battery. The grid return is connected to the movable arm of this unit. When oscillations start, the arm is thrown to the positive side of the potentiometer so that considerable grid current flows. This lowers the in put resistance of the tube and decreases the resistance across the tuned circuit, which is the same as adding series resistance to it. And so oscillations cease again.

These methods decrease the amplification at the same time they decrease the oscillations. The potentiometer method also consumes considerable B battery current because of the high plate current when the grid is positive, and is none too conservative of tube life. At the same time the selectivity of the circuits decreases at a rapid rate.

Other methods, which merely decrease the amplification to the point where the feed-back voltage is not sufficient to produce oscillations, include reducing the A battery filament current, or the B plate voltage. Both of these methods increase the plate resistance of the tube and therefore a smaller a.-c. voltage appears across the plate load.

Another method that has come into common use is the so-called " grid suppressor " method. It involves placing resistance between the tuned circuit and the grid of the tubes. The values of the resistance may be from 300 to 1000 ohms.

260. Bridge systems.—There is another large class of circuits in which unwanted feed-back is fought in another way—a way that seems more scientific to many engineers, although it may be not a great deal more effective. These circuits are the " bridge circuits " of Hazeltine, Rice, Hull, Ballantine, Hartley, and several others.

The Rice circuit is the simplest to understand. It appears in Fig. 195. It involves tapping the input coil in the exact center, and connecting a "neutralizing" condenser from the plate of the tube to the bottom of this coil. If the input coil is tapped at the exact center, and if the neutralizing condenser has the same capacity as the grid-plate capacity, for every voltage fed back through the

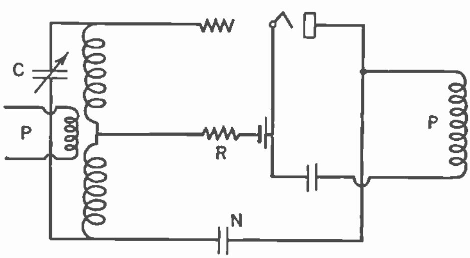


Fig. 195.—Rice neutralized circuit.

latter capacity, of the proper phase to cause regeneration—due to the inductive load in the plate circuit—there will be an equal and opposite voltage fed back through the neutralizing condenser. The equivalent bridge circuit is shown in Fig. 196. If the coupling between the two halves of the input circuit is perfect and if the grid-filament capacity and the filament-plate capacity (in dotted lines) are equal, the bridge will be balanced at all frequencies. Actually these conditions do not exist and so there may be some regeneration, or even degeneration in a given circuit.

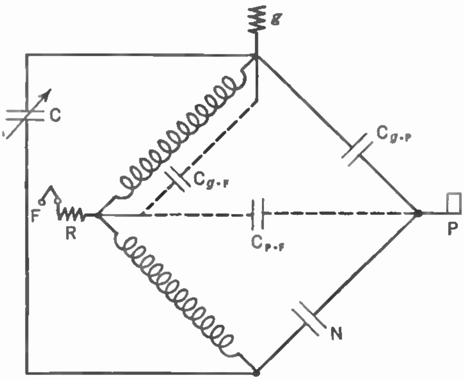


FIG. 196.—Equivalent bridge circuit of Fig. 195.

261. The neutrodyne.—The neutrodyne of Hazeltine gets the neutralizing voltage from the plate voltage instead of the grid voltage as shown in Fig. 197. The Roberts system, Fig. 198, also uses plate circuit neutralization. Other systems are in use, but in general they are more complex than these illustrated here.

The Rice circuit has the advantage that the circuit is complete in itself and no wires need to go to any other circuit for neutralizing voltages. The plate circuit load may be placed at some distance from the amplifier tube itself. It has the disadvantage that half the input voltage is not usefully used, that is, it is not applied to the grid-filament path of the tube. It also has the disadvantage that both sides of the tuning condenser are above ground potential,

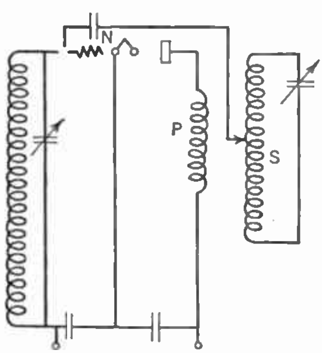


FIG. 197.—Hazeltine neutralized circuit.

one side being connected to the grid and the other to the neutralizing condenser. Some trouble with " hand capacity " will be experienced in using this circuit unless precautions are taken to use a non-metallic shaft on the condenser.

The Rice circuit is troubled with parasitic oscillations, that is, oscillations at some other frequency than those determined by the capacity and the inductance of the tuned circuit. For example, in a Rice neutralized amplifier operating on broadcast frequencies oscillations frequently take place on a wavelength of about 75 meters, corresponding to the inductance of half the input coil and the capacity across it due the grid-filament capacity of the tube, wiring, etc. The other half of the input coil may be thought of as a tickler.

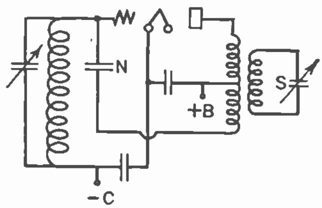


FIG. 198.—"Roberts" neutralized circuit.

A high loss put into this oscillating circuit, as *R* in Fig. 195, will stop all such oscillations. Such a loss may be a high resistance, 500 ohms will do, a choke coil, or an anti-resonant circuit tuned to the offending frequency.

262. Neutralizing bridge circuits.—A single neutralized amplifier is often placed ahead of a regenerative detector by experimenters. In such cases it is only necessary to make the detector oscillate and to so adjust the neutralizing condenser that tuning the input to the r.-f. amplifier does not throw the detector out of oscillation. When such a condition exists, the r.-f. amplifier is independent of its following circuit, and so the detector and the amplifier may be tuned separately to the same frequency without disturbing noises. Actually it is practically impossible to neutralize an amplifier to the point where it will not throw the detector out of oscillation at some frequency. This is because of other couplings that exist in addition to the plate-grid capacity.

If such couplings exist their presence will be indicated by the following test. Make the detector oscillate and pick up a broadcasting station carrier. This will cause a distinct beat note to appear in the head phones or the loud speaker. Now vary the r.-f.

amplifier tuning condenser through resonance with the detector. The beat note will now change. If there are no couplings aside from the grid-plate capacity the tone of the beat note will change to a maximum, or minimum, pitch and then return to its original value. When the tube is properly neutralized this beat note will not change in tone. But if unwanted couplings exist due to wiring, or capacities between plate and grid apparatus, the beat note will have a double hump in it.

The experimenter should not take the exact neutralizing of his amplifier too seriously. All that is really desired is a value of capacity such that oscillations will not take place in the r.-f. amplifier at any frequency within the band that will be tuned over. As a matter of fact a slight misadjustment may increase the strength of the signals.

If an oscillating detector is not present, another method may be used which leads to the same result. The filament of the tube to be neutralized is not lighted. A buzzer-modulated signal is picked up and the neutralizing condenser in this tube's circuit is adjusted until the note of the buzzer as heard in the head phones or loud speaker is a minimum. Then the tube is lighted and the next stage is neutralized in the same manner.

Such a method is faulty in that the plate-grid capacity of a tube is not the same lighted as unlighted, but practically the method leads to stable amplifiers, and this is the ultimate object of neutralization.

263. Filtering r.-f. circuits.—Oscillation is the most serious difficulty which amplifier designers run into. It is caused, as stated above, by coupling part of the plate a.-c. voltage back to the input of the tube. When occurring through wiring, or faulty layout of apparatus, or from one coil to another, it is unpardonable, because it shows evidence of poor design. Let us consider the circuit in Fig. 199. The r.-f. currents should follow the dotted lines, and should go nowhere else. If they do they are sure to get mixed up with similar r.-f. currents from other stages of the amplifier, and thereby cause unwanted coupling. This is analogous to the audio-frequency amplifier problem of keeping a.-c. currents where they belong and out of external circuits.

Filtering of all B and C leads will keep the a.-c. currents in their proper places in the circuit and will keep them from becoming sources of unwanted coupling with other parts of the amplifier. Such a filter may consist of a 5000-ohm resistor in series with the plate battery leads and a fairly large condenser in shunt as shown in Fig. 199. A capacity of 100 mmfd. at 1500 kc. has a reactance of 10^6 ohms and is much to be preferred to a large paper condenser of perhaps 1.0 mfd. capacity which may have considerable inductance in it. Some condensers made of large sheets of paper rolled up together have such an inductance that they present a very high anti-resonant reactance at the higher radio frequencies. For this reason a small mica condenser of 0.01 or 0.001 mfd. capacity will provide good by-passing if the series impedance is fairly high.

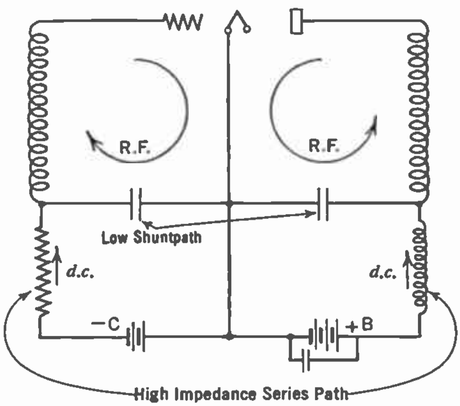


FIG. 199.—Proper use of filtering to keep r.-f. currents where they belong.

Ballantine cites the case of two No. 18 wires two inches apart that have a reactance of 5.8 ohms per foot. A ground wire carrying r.-f. currents and near a grid wire also carrying r.-f. currents or of the proper phase may provide sufficient coupling between circuits to cause trouble from regeneration. No a.-c. currents should be permitted to flow through the filament circuits, or the metallic shields if such are used. Shields should be grounded at only one place, to avoid circulating currents in them.

Magnetic coupling from a plate to a grid coil is a prolific source of unwanted coupling. One method of avoiding this difficulty is to use coils in large and heavy metallic containers which are grounded. Any magnetic field from the coils which would ordinarily become mixed up with similar fields from other circuits (and thereby induce unwanted voltages in them) induce voltages in the grounded shield instead. It must be remembered that the induced voltage is capable of setting up an r.-f. current in this shielding and that the I^2R loss in power in the shields must be supplied from the power in the coils themselves. This results in an equivalent increase in the resistance of the coils inside the shield and a decrease in their inductance. This, of course, decreases the coil's $\frac{L^2\omega^2}{r}$ factor with consequent decrease in both amplification and selectivity. When coils are to be shielded they usually have small diameters and small fields. This construction minimizes the increase in resistance and decrease in inductance.

264. Use of screen-grid tubes as r.-f. amplifiers.—The screen-grid tube will probably remove the necessity for neutralizing radio-frequency amplifiers by removing the source of trouble—the grid-plate capacity. At any rate it is possible to build tubes of this type with such low values of capacity that considerably more voltage amplication can be secured from them without neutralizing than can be obtained from three-element tubes by means of the accessory apparatus already described. It must not be supposed that this new tube—which came into common use in 1929—can be used without danger from regeneration or even oscillation. Any tube with considerable amplification will oscillate provided the circuit constants are correct. If the feed-back due to plate-grid capacity has been eliminated, it does not follow that one can use a circuit set-up in which there may be considerable feed-back from other sources.

Methods of using this new tube will be discussed in Chapter XV. The voltage amplification possible with a single stage may be seen in Fig. 182.

CHAPTER XIV

DETECTION

SUPPOSE we have received a signal and have amplified it in a radio-frequency amplifier. How may it be detected, or demodulated so that it can be put into an audio amplifier and then a loud speaker?

Up to the present time we have considered the applications of the vacuum tube which call for its operation on a straight part of its characteristic where little distortion takes place. We have considered the tube only as an amplifier. We shall discuss now the uses for the curved part of the characteristic.

Tubes act as amplifiers either with or without distortion and as detectors and modulators in which distortion is the essential feature. The latter uses of the tube require a curved characteristic. The output no longer is an exact replica of the input.

265. Distorting tubes.—In Section 188 we were able to calculate the amount of distortion (second harmonics) that resulted when the tube was worked on a curved part of its characteristic, and found that in the distortion process a certain amount of d.-c. current was generated. In other words a pure sine wave voltage put on the grid-filament input of a tube resulted in an output current or voltage composed of not only the frequency that was put on the input but some additional frequencies and some additional d.-c. current as well.

If we desire to get d.-c. current from an a.-c. voltage, the tube acts as a rectifier. If we desire to get audio-frequency voltages from a modulated r.-f. voltage, the tube acts as a detector. If we desire to mix two frequencies, say a low audible frequency with a high or radio frequency, we put them both into a modulator. All of these uses require a non-linear characteristic. Detectors and modulators have three elements just as amplifier tubes have. Tubes designed for rectifiers have only two elements, plate and filament.

266. Modulation.—Consider the circuit in Fig. 200. If the high-frequency generator is turned on and the low-frequency generator is shorted, high-frequency currents will flow in the antenna. Their amplitude will depend upon the amplifying ability of the tube and the amplitude of the applied grid voltage at this frequency. If the grid voltage is of constant amplitude and frequency, the plate current variations and hence the antenna current variations will be of constant frequency and amplitude. Now let us turn on the low-frequency generator. The amplitude of the antenna current will vary and if the proper relations between the plate current and the grid voltage are satisfied the amplitude of the high-frequency antenna current will vary at the frequency of the low-frequency generator.

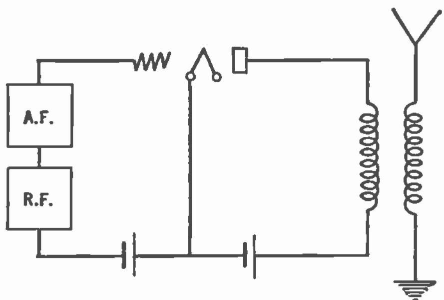


FIG. 200.—A simple modulator.

An idea of how the antenna currents look before and after modulation may be seen in Fig. 201. The high frequency is called the **modulated** or **carrier frequency**, and the low frequency is called the modulating or **side-band** frequency.

Let us call the maximum amplitude of the antenna current B, and its frequency f_c. Then the current at any instant will be $i = B \sin 2\pi f_c t$ in which the "$2\pi f_c t$" takes the place of the phase angle θ but expresses the same thing exactly, namely the amount of time that has elapsed since the beginning of the cycle. Now instead of a constant maximum amplitude B let us vary this amplitude above and below B at some rate, say in the form of a sine wave. The maximum amplitude is no longer constant, but is equal to $B + A \sin 2\pi f_m t$ in which f_m stands for modulating frequency just as f_c indicates carrier frequency. The current at any instant is a function of several variable factors, and may be expressed as $i = (B + A \sin 2\pi f_m t) \sin 2\pi f_c t$.

This process whereby a high frequency is varied in amplitude by a lower frequency is called **modulation.** The system outlined above is called **grid-circuit modulation.** Plate-circuit modulation is explained in Section 363.

The tube in such a process is called a modulator. Once the high-frequency wave is modulated, it acts as a carrier for the low frequency and wherever it goes it takes the modulating frequency with it.

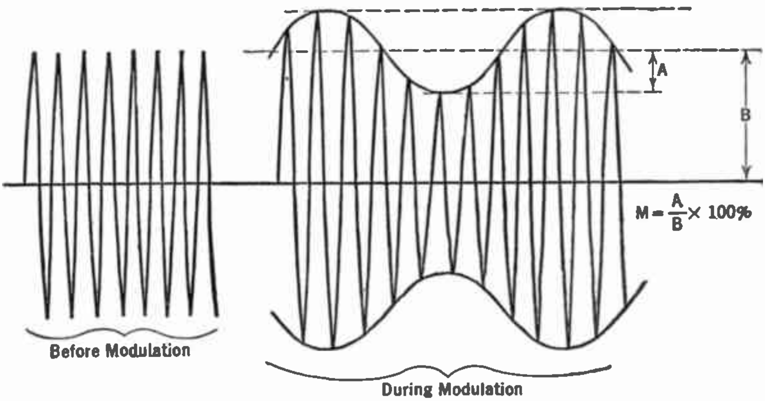


FIG. 201.—Unmodulated and modulated wave.

The depth to which the high frequency is modulated depends upon the relative maximum amplitudes of the two frequencies. If they are equal, the wave is said to be completely modulated, and the "**percentage modulation**" is 100.

267. Percentage modulation.—If the two peak voltages are not the same, the high-frequency wave will not be completely modulated, and the modulation will be less than 100 per cent. In broadcast transmission the modulation rarely exceeds 90 per cent. The greater the modulation percentage the further will the signals from a given station be heard and the greater will be the distortion arising from demodulators or detectors following a "square law." In 1929 the use of "linear" detection became prevalent and it became possible to receive 100 per cent modulation without the "square law" detection distortion.

In Fig. 201 is the carrier before and after modulation. The percentage modulation is defined as the ratio between A, the peak current of the modulating frequency, and B, the peak current of the non-modulated carrier. A glance at Fig. 201 will give a good idea of what is meant by the expression. When 100 per cent modulation is effected, the values of A and B are equal.

$$\text{Percentage modulation} = M = \frac{A}{B} \times 100 \text{ per cent.}$$

268. Demodulation.—If such a modulated wave is turned into a "demodulator," the side-band frequencies can be got back. A demodulator, or detector, acts as though it were made up of two filters, of which one will not pass the high or carrier frequency and the other will not pass the low or modulating frequency. In the demodulator the two frequencies are separated.

A modulator, then, is a device for combining two frequencies. A demodulator, or detector, is a device by means of which we get back from the radio-frequency carrier the modulation or intelligence carrying frequencies.

269. A simple detector.—Let us consider the case of a device which has a response characteristic like XYZ in Fig. 202. When the voltage across it is as large as 4 volts, current begins to flow through it, and from then on the current is proportional to the voltage. Below this value, no current will flow. Now suppose we put an a.-c. voltage on this device. If the average value of the a.-c. voltage wave is at the point A, the same current flows when the voltage is positive or negative—the current wave looks exactly like the voltage wave, just as in the distortionless amplifier. But suppose the average value of the sine wave is at the point B. Then current flows only on the positive halves of the cycle. Such a device is a rectifier or detector and if the operating point is at the exact place where the current begins to flow (as at B), perfect rectification will result.

Now let us consider an unmodulated wave. When it passes into a perfect rectifier, current flows during the positive half-cycle only. Then, if the normal steady current is zero milliamperes, when no a.-c. voltage is applied, this current will become some positive measurable value when the a.c. is applied because, though a meter cannot follow these spurts of current, it will take up some average value between the peak of the spurt and the zero value—which is the same as the normal no-signal value of the current.

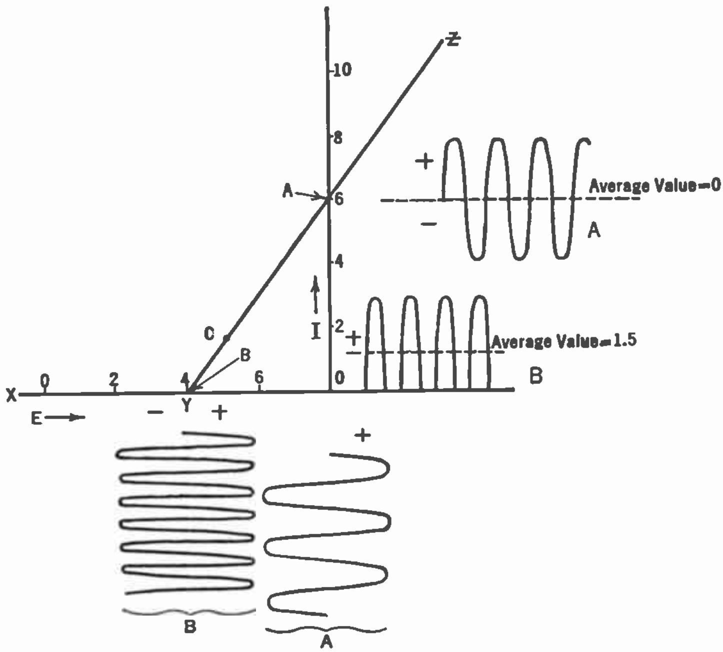


FIG. 202.—Rectification takes place when the operation is at (*Y*) but not at (*A*). Thus the plate current in (*A*) is similar to the input voltage while at (*B*) the output differs from the input.

In such a detector there is an increase in current when a.-c. voltages are applied. Now if the a.-c. voltage is modulated as in Fig. 203, the average value of detector current goes up and down in accordance with these modulations. This varying average value is the useful part of detection since it has the same form as the original modulating voltage and in a distortionless system is exactly proportional to this voltage. This varying value occurs at an audible frequency.

270. The plate circuit detector.—The simplest tube detector is the plate circuit or *C* bias detector, that is, a rectifier which operates upon a curved part of the grid voltage plate current characteristic curve of a tube. It is not a perfect rectifier, but as greater and greater voltages are placed upon it the positive halves of the current waves are much greater than the negative waves, and so the average value of plate current due to rectification increases a corresponding amount.

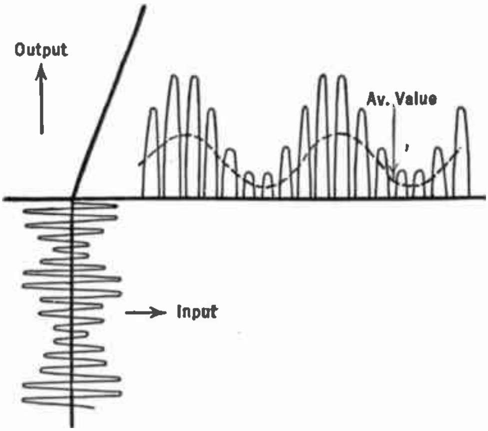


Fig. 203.—Rectification taking place about a non-linear part of a characteristic.

In this process, there are three points to note. First the very rapid radio-frequency variations in input voltage modulated at an audio rate. Each audio cycle is made up of thousands of radio-frequency cycles—only a few of them are shown in the diagrams, for simplicity. When this voltage is placed upon a curved part of the plate curve, the difference between the positive and negative current waves takes the form of the audio variations. Because these positive and negative portions differ in amplitude, the average between them is not zero and therefore the plate circuit contains a current of the frequency of the audio signals. In this process there is an increase in average d.-c. plate current whether the input wave is modulated or not. The plate current meter cannot follow the change in audio plate current and does not indicate whether or not the carrier is being modulated.

271. Detection of modulated wave.—Suppose for example we connect antenna and ground to the grid and filament input of a tube. A nearby station is putting into the ether an unmodulated wave. As soon as we tune to this station's frequency a voltage is developed across the input circuit to the tube; this a.-c. voltage fluctuates the grid voltage, and a change takes place in the average value of the plate current. If the station is powerful enough, and if it is modulated with a key—that is, if its antenna current is started and stopped in accordance to some code—we can use a sensitive relay in the plate circuit of our detector and either read the signals directly from the relay or operate a telegraph sounder with it, or light a lamp, or fire a gun or do anything else which it is required to control by radio. If the transmitted frequency is 1000 kc. it may be necessary to tune the input of the tube to this frequency. A pair of telephones in the plate circuit of the detector, in place of the relay, will indicate by means of clicks when the transmitter started and stopped the antenna current but would not give off any sound in the middle of dots and dashes. If, however, we operated a buzzer with the relay we could read the signals by the audible sound of the buzzer.

We can get around the difficulty of needing a receiving buzzer by having a buzzer or "chopper" at the transmitting station. Now when the key is pressed, the modulated 1000-kc. wave is sent into the ether. If the modulator tone, say 1000 cycles, has a maximum amplitude equal to the maximum value of the 1000-kc. voltage, the antenna current will be doubled 1000 times a second when these two voltages will be in phase. At 1000 other instants the two voltages will be out of phase and the antenna current will be reduced to zero. Across the receiving tube is a 1000-kc. voltage broken up into 1000-cycle sections—modulated as we say.

Now if we place a pair of telephones in the plate circuit of the detector tube, it will offer a certain amount of impedance to these 1000-cycle sections of 1000-kc. currents. A voltage will be built up across the telephones, and our ears will tell us that 1000-cycle signals are being received. The d.-c. plate current meter will still indicate an increase in average plate current when the transmitter key is pressed, but of course its needle cannot follow the 1000-cycle variations. Neither will a relay indicate that the 1000-kc. input is modulated, because it is too sluggish to follow the variations, but it will indicate the average of each section and will close when the key is pressed. The telephones, however, will respond to frequencies as high as 10,000 cycles per second.

If, now, we use a microphone at the transmitter instead of a constant peak amplitude source of tone, like a buzzer, and talk into it the voltage variations impressed on the 1000-kc. voltage may be very complex, perhaps something like Fig. 203 for example. Telephone receivers in the detector circuit will respond to the sections of 1000 kc. but since they are not symmetrical, like a pure sine wave, the receivers will not give off a pure tone. They will give off a note or sound corresponding to what was put into the microphone. If, in the process of detection, other audio frequencies are generated distortion results, because the audio components heard in the telephones are no longer exact replicas of what was put into the microphone. Fortunately these additional frequencies, the strongest of which are of double the original audio tone, are of small amplitude provided the detector is properly operated, and so the tone as heard from the telephone sounds exactly like that put into the microphone.

The process of detection by means of the bend in the plate current curve is essentially one of distortion, in which the r.-f. wave is distorted and out of which we get the audio wave by placing some audio-frequency impedance in the plate circuit of the detector. Usually the plate circuit has a low impedance to the r.-f. a.-c. plate currents, that is, they are by-passed as in Fig. 204, and sometimes an additional precaution is taken to prevent any r.-f. voltages from being built up across the audio impedance in the plate circuit. For example, in Fig. 204 a choke, L, is used.

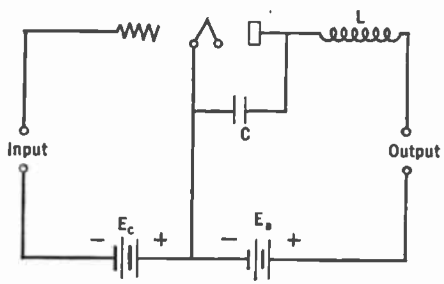


FIG. 204.—To keep radio-frequency currents from the output, a low impedance path (C) and a high series impedance (L) are used.

272. Conditions for best detection.—There are several variable factors in such a detector circuit as shown in Fig. 204. One is the grid bias, E_c, and the other is the plate voltage. Some combination of these two voltages will create the greatest amount of a.-f. voltage across a given impedance when a given r.-f. voltage is put on the grid. The *C* bias is governed to some extent by the amplitude of the r.-f. voltages to be put on the grid of the tube.

If an r.-f. voltage of 1 volt maximum is to be impressed on the grid of the tube, a *C* bias of slightly over this value will take care of the signals and offer a certain margin of safety. The problem then is to find the plate voltage that will put the operating point at a place of great sensitivity. Values for an ordinary tube of the 201–A type are about minus 4.5 with a plate voltage of 45 and minus 9 with a plate voltage of 90.

In such a detector the greater the r.-f. voltage the greater the change in average plate current and the greater the audio signal in the output load. With a given r.-f. voltage the audio signal will be proportional to the amount of modulation at the transmitter. That is, if the power from the radio oscillator at the transmitter is constant but the voltage coming from the microphone varies, the audio notes at the receiver should vary in exact proportion to the microphone notes.

Otherwise there is distortion. The audio notes with a fixed modulation vary approximately as the square of the r.-f. voltage when the latter are small. That is, doubling the radio-frequency voltage across the antenna will result in multiplying by 4 the audio tones from the detector. Actually the square law holds only over the certain small part of the plate current curve, for example: for low input signal voltages. The law is less than a square function for large input voltages. The change in d.-c. current (increase) is independent of the modulation and a meter in the plate circuit will not tell whether or not the r.-f. input is being modulated.

273. The vacuum tube voltmeter.—The detector may be calibrated and used as an a.-c. voltmeter. Such vacuum tube voltmeters are useful at all audio and nearly all radio frequencies, and can be made to read d.-c. voltages. The range of voltages that can be measured is very large, the upper limit being the voltage the tube can stand without breaking down, and the lower limit depending upon the sensitivity of the indicating instrument.

The principle of such devices is simple. The operating point is chosen, by adjusting the *C* bias and the plate voltage, so that it is on a point of considerable curvature. When an a.-c. voltage is put on the grid, rectification takes place in the plate circuit, and the d.-c. part of the rectification product is read on a d.-c. instrument. If the voltmeter is properly biased, its input resistance is very high and it takes so little power from the device whose voltage is being measured that it may be considered as having no effect upon the circuit.

The choice of *C* bias depends upon the input voltages to be measured. Let us suppose we are to measure a peak voltage of 5 volts. Clearly the *C* bias cannot be less than this because of the decreased input resistance when the grid draws current and the effect of such a meter upon the circuit under measurement. The *C* bias would be some value over 5 volts, 6 for example. The next step is to fix the plate voltage. This is determined by the range in input volts to be measured, and the kind of instrument used to read the d.-c. current. For greatest accuracy E_p should be such that the greatest deflection of the current meter will be obtained by the given input voltage. In general a voltage range of about 5 to 1 is all that can be read with an ordinary voltmeter, that is, from about 0.5 volt to 3.0 volts. The problem then is to choose a plate voltage that will enable the desired range to cover completely the scale of the meter being used.

For measurements of average voltages, say up to 10 or 15 volts and as low as 0.5 or 1.0 volt, a microammeter reading 200 microamperes and costing about $35 is a good instrument. A small laboratory model of milliammeter reading 1.0 or 1.5 milliamperes can be used although the accuracy of measurement will not be so great as with a more sensitive instrument.

274. Adjusting a voltmeter.—What is desired is the greatest change in plate current with a given a.-c. voltage. In Fig. 205 are some curves taken with a 3-volt, 60-milliampere tube, showing the plate current at various values of a.-c. grid voltage and at various values of plate voltages. The change in plate current, that is, the value *with* a.-c. input voltage minus the value *without* input, is plotted and shows the futility of using plate voltages greater than 35 volts when sensitivity is the criterion.

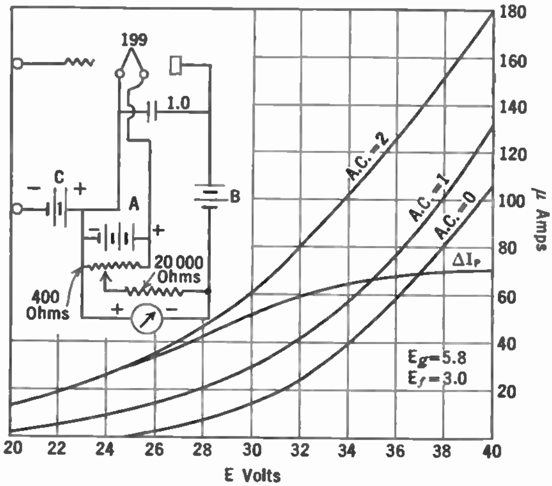


FIG. 205.—Calibration and circuit of vacuum tube voltmeter

Because the tube takes some plate current even when there is no a.-c. grid voltage, part of the scale of the d.-c. meter is taken up with this steady reading. This reading can be balanced out by means of the zero adjuster on the meter, or by using another current through the meter in such a direction that the original plate current is "bucked out." The whole meter scale is available then for plate current changes occurring under input grid voltage excitation. Such a balancing out voltage may come

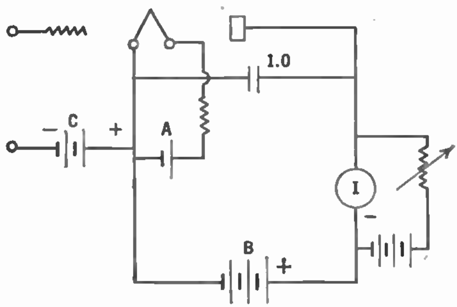


FIG. 206.—Method of balacing out the steady plate current from the indicating meter.

from an additional battery and adjustable resistance, as in Fig. 206, or from the voltage drop across the tube filament as in Fig. 205.

Experiment 1–14. Use of the Vacuum Tube Voltmeter.—There are two types of vacuum tube voltmeter: the *C* bias type and the grid leak and condenser type. The latter is more sensitive but draws current from the device whose voltage is being measured. Both types should be experimented with. They are the most versatile and useful of all radio instruments.

Connect up a *C* bias voltmeter using a 0–5 milliammeter in the plate circuit, about 45 volts on the plate, and add sufficienct *C* bias to decrease the plate current to nearly zero. Then use a more sensitive plate current meter, and a bucking battery to reduce the deflection to zero. Calibrate the meter by putting known currents through known resistances at 60 cycles or at any radio frequency. With 45 volts on the plate and about 9–13 volts *C* bias with average tubes, voltages as low as 1.0 will give a good deflection and peak voltages up to about 7.0 can be read on a meter reading about 1.0 milliampere.

Fairly accurate calibration may be performed by using the voltages available from a filament current transformer, that is, 1.5, 2.5, and 5.0, and of course combinations of these voltages depending upon how the windings are connected together.

Connect the voltmeter across the tuned circuit of a radio-frequency stage, or across the coil-condenser combination that can be coupled to an oscillator. Tune the condenser and note how the voltage across the coil increases through resonance. Insert some resistance into the tuned circuit and repeat. Note how much broader the resonance curve is and how the minimum voltage has decreased.

Connect the voltmeter across the resistor of a resistance-coupled amplifier tube—inserting a large capacity between the plate terminal of the amplifier tube and the grid of the voltmeter so that the d.-c. voltage across the resistor will not bias the grid of the voltmeter. Apply a known voltage to the input of the amplifier and measure the output voltage. Then change the plate resistor and again measure the output voltage. Plot a curve showing amplification against plate load resistance.

Place the voltmeter across the secondary of an audio transformer and apply a known voltage in series with a resistance of about 15,000 ohms and the primary. Measure the turns ratio of the transformer at 60 cycles or some other frequency by measuring the secondary voltage.

These are but a few of the many experiments that can be performed with the vacuum tube voltmeter. It can be used to measure field strength of distant transmitters, resistance of coils, amplification of amplifiers, resonance curves, frequency characteristics of amplifiers, etc.

275. D.-c. plate current as a function of a.-c. grid voltage.—The vacuum tube voltmeter is really a *C* bias or plate circuit detector, and the change in plate current is a function of the a.-c. voltage on the grid. It is only necessary to calibrate the detector, using any source of a.c. and any standard a.-c. voltmeter as a standardizing voltage, or a known current can be passed through a known resistance and the voltage drop used for calibration.

The detector in one's radio is also a vacuum tube voltmeter although it is not so calibrated. If a sensitive meter, say reading up to 5 milliamperes, is placed in the detector plate circuit of any radio receiver, changes in the reading will be noted when a strong signal is tuned in. If the detector is a grid leak and condenser type, the reading will decrease. If greatest sensitivity is desired, the steady no-signal current may be balanced out and then a sensitive microammeter may be used. The changes in this meter reading may serve as a measurement of fading, signal strength, etc. No change will occur unless the r.-f. voltage on the input to the tube changes. Modulation will not cause any change unless the transmitter is over-modulated. Generally speaking an r.-f. signal at ordinary modulation percentages causing a change in detector plate current of 100 microamperes will, with two stages of audio amplification, deliver a good loud speaker signal.

276. Detection in a radio-frequency amplifier.—Because the r.-f. stages of a receiver are biased, it often happens that some detection takes place in one or more of them, probably in the first. What happens is something like the following: the first tube is so biased, and may have such a low load impedance in its plate circuit at the frequency under consideration that the operating point is on a part of considerable curvature. Now a strong signal comes in, a large a.-c. voltage is impressed on the r.-f. grid and detection is the inevitable result. A pair of receiving telephones in the plate circuit of this tube would have an audio-frequency voltage across them, due to the rectified voltage, and would give an audible response.

For example suppose the receiver is tuned to a frequency of 600 kc. This means that the load impedance in the plate circuit of the r.-f. amplifiers will be high at 600 kc. but low to all other frequencies. The tube will have a curved characteristic to any signal of higher frequency than this. A powerful local station on some other frequency puts a strong signal on the grid of the r.-f. tube, and the rectified voltages modulate the r.-f. voltage of the 600-kc. wave so that what gets into the second r.-f. stage is a 600-kc. signal modulated with what is going on at the studio of the other station. The modulation of the distant station may be inaudible.

A wave trap tuned to the offending local station is a good remedy for such trouble.

277. Grid leak and condenser detector.—In the plate circuit detector, we may look upon the signal as having first been amplified by the tube and then as going through the detection process when it reaches the plate circuit. There is little amplification in such a tube at r.f. because of the low plate circuit resistance at r.f. There is another type of detector more complex in theory and more sensitive which is in more common use. This is the familiar grid leak and condenser detector shown in Fig. 207. In this case we may think of the r.-f. signal as going through the demodulation or detection process in the grid circuit of the tube and then having the resulting audio tones amplified in the plate circuit just as in an ordinary amplifier. Because of this amplification, this type of detector is more sensitive than the *C* bias type.

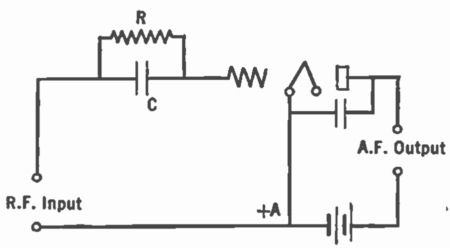


Fig. 207.—Grid leak-grid condenser detector.

Such a tube detects on its grid-current curve, and so the grid voltage must be such that the operating point is on a curved part of the grid-voltage–grid-current curve, and because it amplifies on its plate-current curve the plate voltage must be fixed so that the operating point is on a straight part of the plate-current curve.

The grid current plotted against grid voltage of a 201–A type tube is given in Fig. 208. It will be noted that even though the grid is negative a certain amount of grid current flows. This is due to the few electrons which leave the filament with sufficient velocity to get to the plate even through the negative retarding force of the grid. This grid current must flow through the grid leak, usually of the order of from 1 to 10 megohms. The voltage drop across this resistance is such the the grid end is negative with respect to the filament even though the " grid return " is connected to the

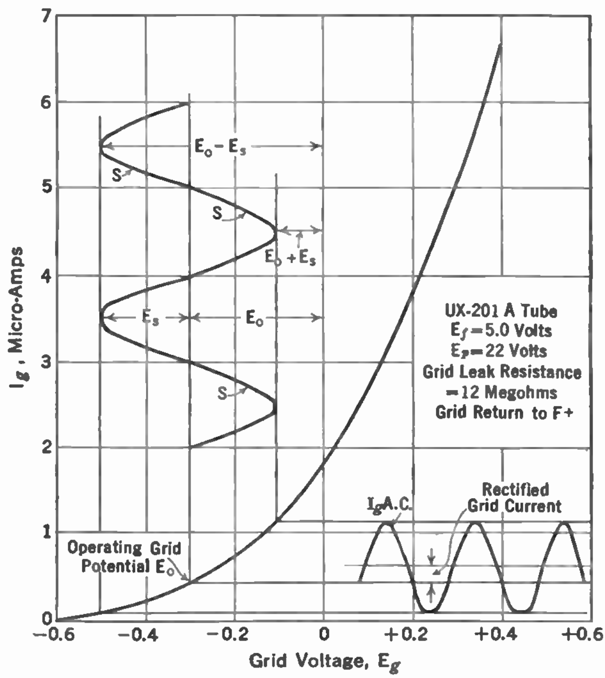


FIG. 208.—Rectification on the grid voltage-grid current curve.

positive end of the filament battery. The value of the grid leak fixes the point on the grid-current curve at which the input signals operate. In Fig. 208 the operating point is about 0.3 volt negative. A higher grid leak has a greater voltage drop across it and so the operating point is somewhat more negative, but the entire range of grid-leak values that are used does not vary the operating point more than 1 or 2 volts.

278. Effect of grid leak and condenser values.—Changes in grid leak value produce no other change in the detector action than is produced by changing the operating point. This is the entire purpose of the grid leak. The purpose of the grid condenser is to by-pass the high resistance so far as r.-f. currents are concerned so that the greatest possible r.-f. voltage may be built up across the grid-filament input of the tube. If the condenser is too small, there will be an appreciable r.-f. voltage loss in it, and the tube will not get all possible of the input signal. If the grid condenser is too large, the audio-frequency voltages built up across the grid leak will be by-passed. The grid condenser with modern types of tubes should never be greater than 0.00025 mfd. and a value of 0.0001 may be used satisfactorily. Smaller condensers than this produce some loss in r.-f. voltage, and result in decreased sensitivity.

279. Detector action.—When an input signal is applied to the tube the grid voltage changes in accordance with the incoming signal just as it does in the case of an amplifier or a plate current detector. These changes in grid voltage produce a change in grid current in accordance with movements up and down on the curve of Fig. 208. Because of the curvature the grid current increases more when the grid is positive than it decreases during the negative half-cycles of input voltage. The result is a net change in grid current, in this case an increase. This increase in grid current produces an increased voltage drop across the grid leak and a greater negative voltage in the grid. This increase in bias causes a *decrease* in plate current. It will be remembered that an input signal caused an *increase* in plate current in the plate circuit detector. These audio grid current changes produce corresponding plate current changes whence they are passed on to the audio amplifier.

In practice, then, modulated r.f. voltages are put on the input to a detector; within this detector the modulations are separated from the carrier that brought them to the receiver; and finally these modulations in the form of a.f. frequencies are applied to a plate-circuit load—usually the input to an a.f. amplifier.

How this separation of carrier from modulation takes place, and how much a.f. one gets out of a given detector with a given input modulated at a given percentage may be determined experimentally as follows. We may fix upon some grid bias voltage, e.g., in the case of a *UY* 227 about 18 volts with a plate voltage of 180. Then we can put on the input to this tube, operating as an overbiased amplifier, or detector, various alternating voltages which need not be at radio frequencies. These input voltages

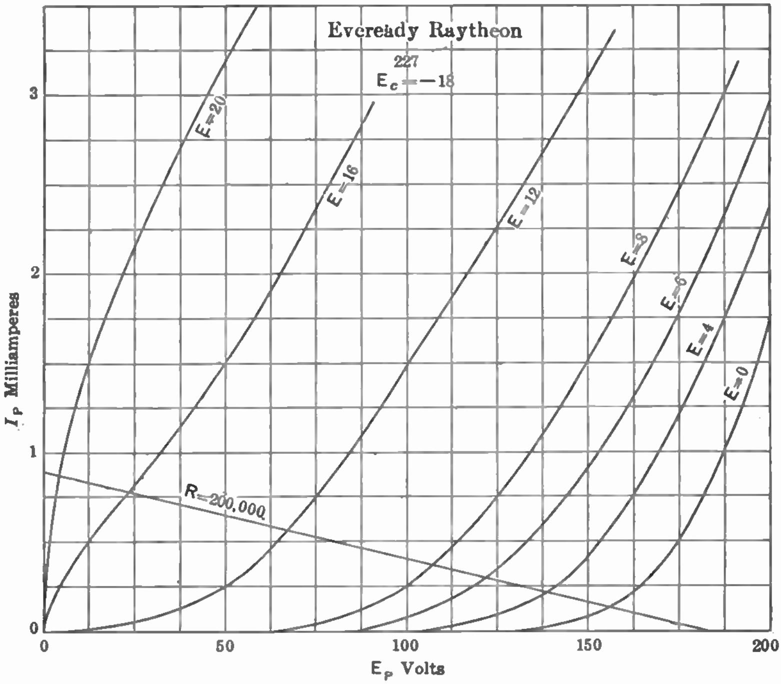


FIG. 209.—Plate current curves as controlled by plate voltage and input carrier voltage applied to grid.

cause some change in plate current which may be read with a fairly good milliammeter. All that is needed then to experimentally determine the detection characteristic of a *C*-bias detector is a source of known alternating voltages and a good milliammeter.

Such a series of curves are shown in Fig. 209. For example with 100 volts on the plate, an input alternating voltage of 12 produces a plate current of 1.5 milliamperes. Across such a family of curves a load line (see Section 186) can be drawn for any load resistance, in this case 200,000 ohms. This is about the highest resistance load that can be used because of various capacities which will shunt it and reduce its impedance at the higher audio frequencies.

The rectified output voltage of the detector, e.g., the a.f. voltage applied across the 200,000 ohm resistor and hence to the input of the a.f. amplifier, can be obtained from such a curve. For example with an input of 12 volts ($E = 12$) the rectified voltage may be found by noting the intersections of the load line with the $E = 0$ line and with the $E = 12$ line. Thus the rectified voltage is the difference between $E_p = 156$ (intersection with $E = 0$) and 66 (intersection with $E = 12$) or 90 volts. Taking several of such voltages a curve like that in Fig. 210 can be plotted.

Now this curve gives not only the rectified voltage due various values of *carrier* voltage but by knowing how strongly this carrier is modulated, the actual a.f. voltages applied across the load resistance may be ascertained. For example, if the plate voltage is 300 and $E_c = 27$ volts, suppose a carrier voltage of 12 is modulated 33 per cent. The carrier voltage will then vary between $12 - 12 \times 33$ per cent and $12 + 12 \times 33$ per cent or between 8 and 16 volts. These values of carrier voltage represent rectified voltages of 47 and 124 and because the carrier swings as far up as it does down from its unmodulated value of 12, the audio voltage produced by these variations is $\frac{124 - 47}{2}$ or 38.5 volts.

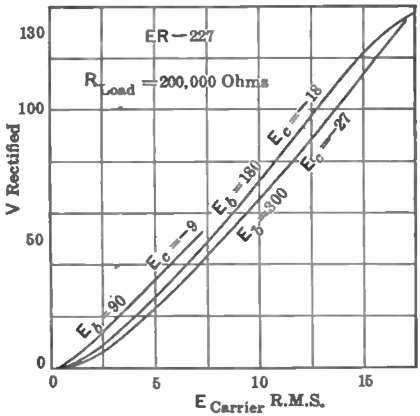


Fig. 210.—Plate rectification "power" detector characteristic.

280. Power detection.—Because of distortion and hum arising in audio amplifiers some designers believe it advisable to do away with at least one stage of audio amplification. During 1929 many receivers were developed which had only one stage of audio amplification and the expression arose of "power detection," meaning that the detector put out enough a.-f. voltage to "load up" the final power tube in the receiver. How is this done? What is a power detector?

A power detector is simply a detector that will not overload when very large r.-f. input voltages are applied to it and which will turn out considerable power in its output. Here again there are two kinds of detectors, the grid leak and condenser and the *C* bias. The *C* bias is the more common type; it is simply a highly biased tube. Even a power detector can distort; on Fig. 210 if the lines curve appreciably, equal carrier voltage swings will not produce equal a.c. voltage swings.

281. Distortion from square law detector.—It is an advantage from the standpoint of efficient use of transmitting power to keep the modulation at the transmitter as high as possible. It is an unfornate fact, however, that with square law detectors the distortion appearing in the output of the detector—due to second harmonics generated in the tube—increase as the square of the modulation. They are proportional to $M^2/4$ where M is the percentage modulation. Thus when an r.-f. wave is modulated 100 per cent there are 25 per cent second harmonics present in the detector output.

With linear detectors high percentages of modulation can be used without this second harmonic distortion, and it is probable that all good broadcasting will use high modulation as more receivers employ linear detection.

The advantages of power detection are: (1) possibility of linear detection and consequent decrease in distortion; (2) ability to do away with one stage of audio amplification and the distortion that occurs in it; (3) shifting amplification from audio to radio decreases noise both from hum and from tube noise itself; and (4) decreased expense due to decreased filtering problem and decreased cost of audio system.

A power detector can be arranged to overload before the final power tube, or any other tube, in the receiver. Since the output of a *C* bias detector decreases when its grid is forced positive, the output from such a detector actually falls off with increase in input beyond the overloading point. Thus it is possible to make the distortion from such a receiver actually less for a strong signal than

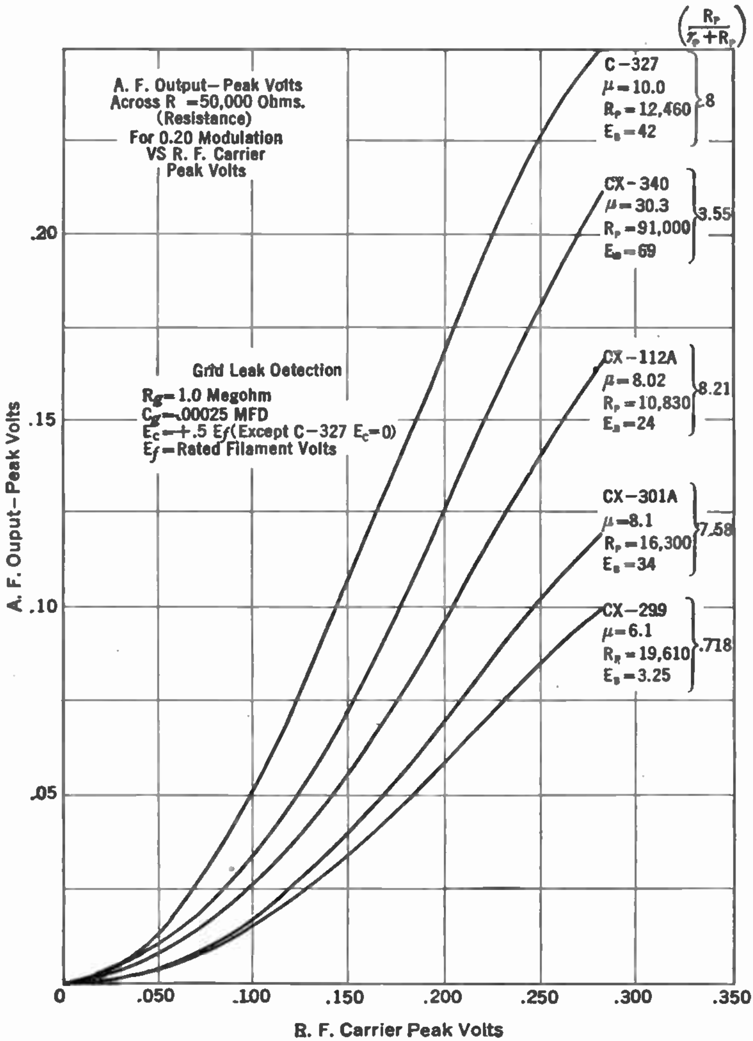


FIG. 211.—Comparison of various tubes as grid leak detectors.

for a weak one. In Fig. 213 will be found a curve showing how the percentage distortion from the Crosley Jewelbox receiver (1929)

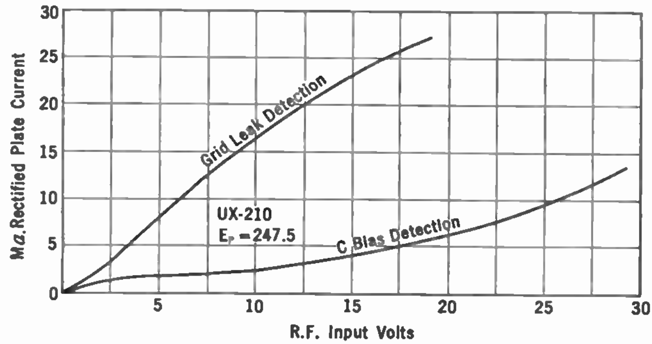


FIG. 212.—Comparison of grid leak and *C* bias detection.

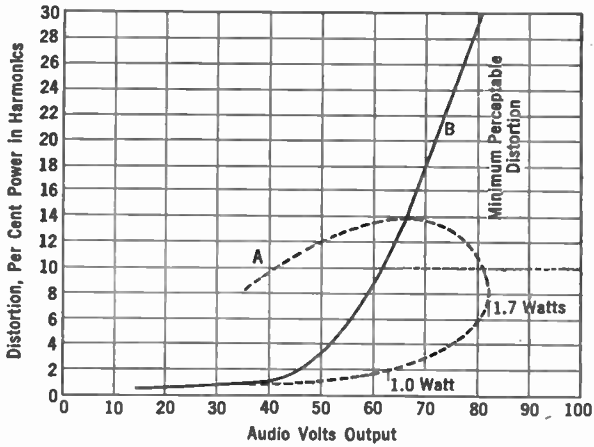


FIG. 213.—Overload characteristic of 1929 receiver. Increasing the input to the amplifier to the detector-amplifier beyond the overload point results in a decreased output (*A*). In older sets (*B*) distortion increases as input level is raised.

falls off with greater output voltage whereas that of the conventional grid leak and condenser detector (*B*) not only increases rapidly with output voltage but begins to overload at a much lower output.

CHAPTER XV

RECEIVING SYSTEMS

There are three types of receiving circuits: (1) The tuned radio-frequency receiver, neutralized or not; (2) the superheterodyne; and (3) the receiver, like the Sparton, in which the processes of selection and amplification go on independently of each other.

282. The tuned radio-frequency set.—The tuned r.-f. set of as late as 1928 suffered from various faults: poor selectivity at high radio frequencies, and excessive selectivity and poor gain at low radio frequencies. In 1929 manufacturers began to look seriously upon these faults with the result that the overall amplification curves began to flatten out and the selectivity curves at 1500 kc. began to look more like those taken at 550 kc. Some such receivers still suffer from excessive sharpness of tuning so that higher audio frequencies are cut off. The fact that tuning a receiver by variations of inductance reverses the faults possessed by a receiver tuned by capacity, is used by several manufacturers to bring up the amplification at low radio frequencies to a level comparing with the gain at the higher frequencies. Others have other tricks to make the response curve flat from 550 to 1500 kc.

283. The superheterodyne.—The double detector or superheterodyne receiver operates on a very interesting principle. Theoretically is seems to have almost every advantage that other receivers possess and some in addition. Practically it suffers from some faults.

It is more difficult to get high amplification at broadcast frequencies than at frequencies of the order of 30–200 kc. without resorting to several stages, neutralizing circuits, careful shielding, etc. Much greater amplification per stage can be obtained at lower frequencies. If, then, we can change an incoming frequency of say 1000 kc. to 100 or even 50 kc., we can get as much amplification in two stages as are obtained from four stages at the original frequency. This means simplification in apparatus, and because of the lower frequencies the problems of stability and shielding are also simplified. An additional advantage lies in the constant band width passed by the amplifier, regardless of the frequency of the incoming signal. How is such a frequency change performed?

284. The phenomenon of beats.—Suppose two loud speakers are attached to two oscillators, one generating a 1000-cycle tone and the other an 1800-cycle tone. When these two tones enter the ear, the listener hears not only the two individual tones but an 800-cycle tone too. If one of the two original tones is modulated at another frequency, say 50 cycles at a given per cent, this 800-cycle tone will be so modulated. By turning this modulated 800-cycle tone into a demodulator, the 50-cycle modulations can be got back.

The two frequencies above are said to **beat** with each other and the difference frequency is called the **beat note.** If the two oscillators are adjusted so that they are at **zero beat** they have the same frequency and no beat note will be heard. In addition to the two beating frequencies and the difference of the two (the difference or beat frequency) there is a third frequency generated. This is the sum of the two beating frequencies. It is called the sum frequency. Thus in the above case there are in the ear 1800-, 1000-, 800- and 2800-cycle tones.

Now suppose we are receiving a 1000-kc. signal and want to turn it into a 100-kc. signal. All we need is a local oscillator which turns out either 1100-kc. or 900-kc. signals. We turn these two signals into a mixing tube where the difference or beat frequency is generated, put its output through a filter which cuts off everything but the 100-kc. signal (which is now modulated at the same modulations as the incoming 1000-kc. signal), and amplify it in an **intermediate-frequency** amplifier. After sufficient amplification has been attained the 100-kc. signal is put through a demodulator and the original microphone modulations secured. These frequencies can be put through an audio-frequency amplifier of conventional design and the output finally put into a loud speaker. The system is shown in Fig. 214.

285. Superheterodyne design.—Some superheterodynes use a stage or two of radio-frequency amplification ahead of the frequency changing system; others do not. Some have sufficient amplification so that the input voltages are taken from a small loop; others require an antenna of conventional form and size. Some have one, two, or three stages of intermediate amplification. In some the function of oscillation and frequency mixing goes on in the same tube; in others these functions are separate. Some systems amplify the sum of the two beating frequencies; most of them utilize the difference frequency. Some have high and some

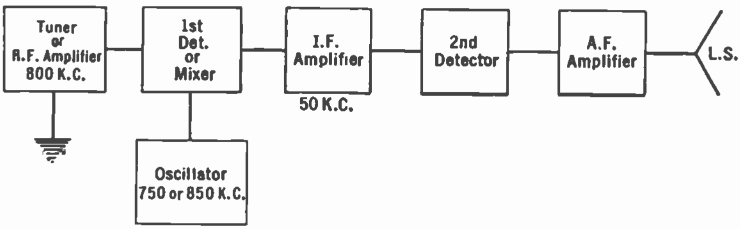


Fig. 214.—Symbolic diagram of superheterodyne.

low intermediate frequencies. Some use *C* bias detection and some use grid leak and condenser detection. Some use air core and some iron core intermediate transformers. And so on. Every designer has his own ideas of which is best, or which avoids patents held by some other designer. In one receiver of this type the beat frequency was secured from mixing a locally generated second harmonic of the incoming frequency with the signal frequency.

In all of the double detector receivers, the signals must first be received and usually tuned—whether amplified or not—at the frequency of the incoming signals. Then the mixing with the local oscillator goes on, either in a separate tube—the first detector—or in the oscillator tube, and then the unwanted products consisting of the beating frequencies, etc., are filtered out. There need be no more than two dials, one tuning the input circuit to the incoming signal and the other tuning the oscillator until it is within the required intermediate frequency of the incoming signals. This produces the beat frequency which is passed through the intermediate amplifier.

Modern design has eliminated one of the dials, so that both the tuning process and the adjusting of the oscillator to produce the required difference frequency are controlled by the same dial.

286. Radiola 60 series.—The curves given here are among the few that have been presented in the radio literature on receivers of this type. The data are representative of the Radiola 60 series and were presented in a paper before the Institute of Radio Engineers in March, 1928, by G. K. Beers and W. L. Carlson, of the Westinghouse and General Electric Companies respectively.

This receiver series is composed of a tuned broadcast-frequency amplifier, and a detector similar to a receiver of the T.R.F. type, followed by an intermediate amplifier and second detector which drives the single stage of audio amplification. The intermediate frequency is 180 kc., keeping out of the second detector and the loud speaker tube hiss and other extraneous and unwanted noises which frequently pass through a lower-frequency amplifier which acts to them as any radio amplifier would.

The radio-frequency amplifier differs from other amplifiers in that the primary of the coupling transformer is larger than the secondary. Although other transformers have small primaries whose natural frequency is higher than any frequency that is to be received, these transformer primaries are so large that they resonate to a natural frequency lower than any frequency to be received. At the lower broadcast frequencies, where most receivers are insensitive, this amplifier has somewhat greater gain and better fidelity characteristics. Where the old and small primary increased the effective secondary resistance at the higher frequencies and thereby made tuning broader there, the new primary makes the tuning broader at the lower frequencies and pulls up the the amplification somewhat there, at the same time reducing it somewhat at the higher frequencies. The result is a flatter amplification curve as shown in Fig. 215. This scheme has been developed by the Hazeltine laboratories for coupling the receiver to the antenna. Better response at low radio frequencies is thereby obtained.

Because of the higher inductance of the primary it has a capacity reactance at all frequencies in the broadcast band, and being in the plate circuit causes the tube to "degenerate," that is, to reduce the input voltage because of the grid to plate capacity just as an inductive plate load causes the tube to regenerate. (See Section 258.) A small condenser acting as a neutralizing condenser reduces the degenerating feed-back voltage and maintains the voltage gain.

The plate and grid coils of the intermediate amplifier transformer are both tuned and so coupled that the response curve is broadened out, thereby providing a better transmission character-

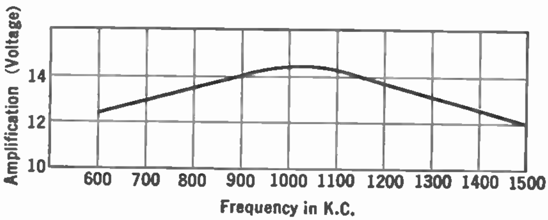


Fig. 215.—Amplification-frequency characteristic of r.-f. amplifier in Radiola 60—gain per stage

istic by not suppressing side-bands as badly as many of the amplifiers of the past. The overall response curve of the intermediate frequency amplifier is given in Fig. 216.

The second detector characteristic is illustrated in Fig. 210. It is a UY–227 with 180 volts on the plate and 25 volts bias on the grid. It is a power detector of the *C* bias type.

287. "Repeat points."—Many superheterodyne receivers suffer from "repeat points," or the fault of getting a station at two settings of the oscillator dial, or getting two signals with a given setting of the oscillator dial.

Let us suppose the beat frequency is to be 50 kc. At 550 kc. the frequency of the oscillator can be either 600 kc. or 500 kc. to provide this beat frequency of 50 kc. At 1500 kc. the oscillator can be set at either 1550 or 1450 kc. This means that the range in frequency of the oscillator must be from 500 to 1450 kc. or from

600 to 1550 kc. Let us receive a station operating on 550 kc. If the oscillator frequency range is from 500 to 1450 kc., the 550-kc. station can be heterodyned at two oscillator dial points, either at 500 or 600 kc. The 1500-kc. station can be heterodyned at only one point, namely, 1450 kc., because it does not tune as high at 1550 kc.

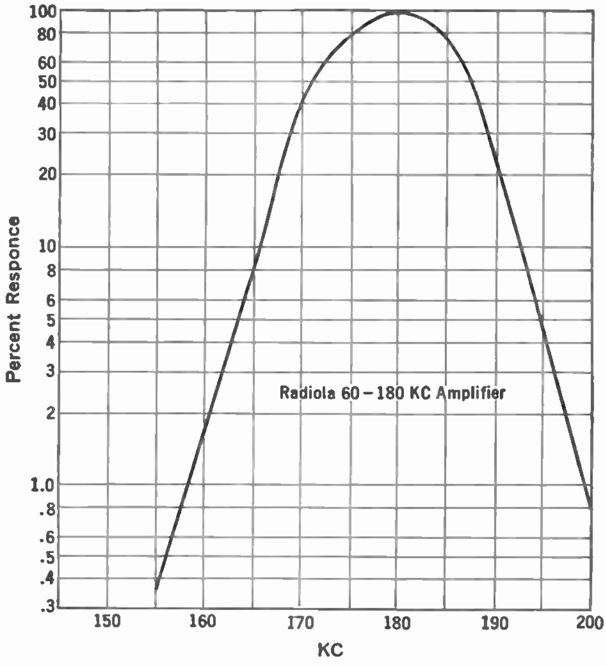


FIG. 216.—Response of intermediate frequency amplifier of Radiola 60.

On the other hand, if the oscillator range is from 600 to 1550 kc., the 550-kc. station can be heterodyned at only one oscillator dial setting corresponding to 600 kc. because it does not tune as low as 500 kc., but the 1500-kc. station can be heard at two points, either 1450 or 1550 kc.

No matter which range the oscillator covers, stations operating anywhere between 550 and 1500 kc. can be heard at two points;

thus an 800-kc. station can be heterodyned by setting the oscillator at either 750 or 850 kc.

Now let us suppose the oscillator frequency is set at 750 kc. If there are two stations, operating at 700 and 800 kc., equally powerful at the input to the receiver, both will provide the required 50-kc. intermediate frequency and both will be received.

In two-dial receivers of this type, some discrimination against unwanted stations is had by tuning the input circuit to the desired station. Thus if the oscillator is tuned to 750 kc. and the input circuit to 700 kc., the 800-kc. station would be tuned out and would not affect the receiver.

But in single-control receivers both the input and the oscillator are tuned at the same time. If, then, the control dial is set at some point, two stations differing in frequency by twice the intermediate frequency (in this case by 100 kc.) and equidistant (in frequency) from the oscillator frequency will be received with equal strength. This is because it heterodynes both of them by the required 50-kc. frequency.

There is another cause for repeat points. If the oscillator generates harmonics, they may heterodyne a higher frequency incoming signal according to the following reason. Suppose the oscillator is set at 600 kc. but generates a strong second harmonic, 1200 kc. This harmonic will provide the proper 50-kc. beat note with either a 1150- or a 1250-kc. station at the same time the fundamental heterodynes a 550 or 650 station. Such harmonics can be reduced by making the oscillations feeble by reducing the plate voltage or by placing a large resistance in the plate circuit to make its characteristic straight, or by giving the grid the proper bias.

Let us suppose now that the beat frequency is 600 kc. The oscillator frequency range must be from 550 plus 600, or 1150 kc., to 1500 plus 600 or 2100 kc., and there will be no repeat points due to heterodyning two incoming signals to give the required 600-kc. beat frequency.

The use of a radio-frequency amplifier ahead of the frequency system will provide considerable discrimination against unwanted stations. It must be tuned to the required station at the same time the oscillator is tuned so that it gives the required beat frequency. If the radio-frequency amplifier provides a 40-DB discrimination against a station 20 kc. away from the desired station, it will keep out of the remainder of the receiver signals from undesired stations even though their frequency difference is correct to pass through the intermediate amplifier.

288. Choice of the intermediate frequency.—If the intermediate frequency is high there will be some difficulty in getting a high voltage amplification. If the frequency is low, the amplifier will probably transmit high audio-frequency noises originating within the radio circuit. The high-frequency amplifier will suffer from stray couplings between stages, and therefore will be difficult to control. The low-frequency amplifier will make impossible complete isolation of the oscillator and input circuits which are tuned to within a few kilocycles of each other.

In the Radiola 60 series, the intermediate frequency is chosen at 180 kc. as a compromise betwen these two difficulties.

289. Selectivity of superheterodynes.—In addition to the selectivity provided by the r.-f. amplifier, there is some selectivity added in the intermediate-frequency amplifier. Let us suppose the desired signal gives the required 180-kc. beat frequency which, according to Fig. 216, gives 100 per cent response. An unwanted station operating at 20 kc. off the desired frequency is also heterodyned by the oscillator, but instead of producing a beat frequency of 180 kc. it produces either 160 or 200 kc. According to Fig. 216 these signals would be reduced to about 1.0 per cent of the desired signal. This is an additional discrimination of 40 DB which added to the 40 DB secured in the r.-f. amplifier provides a total selectivity of 80 DB.

Problem 1–15. If the intermediate frequency of the Radiola 60 is 180 kc., what must be the range of the oscillator frequency to produce this beat frequency at broadcast frequencies?

290. Frequency changers.—Any tuned r.-f. receiver can be converted into a superheterodyne by the addition of an oscillator and a mixing tube. In such a system the r.-f. amplifier is used as the intermediate-frequency amplifier, and is set to give maximum amplification at some fixed frequency within the broadcasting band. Then the oscillator beats with the incoming signals so that this frequency is generated and the signals are finally detected in normal manner.

291. The "autodyne."—It is possible to do away with one tube by combining the functions of oscillator and mixing tube, or first detector. It is only necessary to couple the input circuit, the antenna-ground system for example, to the oscillator which acts as detector. The latter is tuned so that its frequency differs from the incoming frequency by the number of kilocycles to which the intermediate amplifier is tuned. Such a "super" is called an **autodyne** because the signal is automatically heterodyned in the local oscillator, or first detector, instead of requiring a third or mixing circuit.

292. "Short-wave" receivers.—The majority of the traffic carried on in the higher frequency bands, from 1500 to 15,000 kc., is in code and it is not necessary to transmit a very wide range of frequencies to convey good signals. In speech the frequency band must be at least 5000 cycles wide, in transmitting music the band should be 5000 each side of the carrier frequency or a band of 10,000 cycles. For code transmission the width of band required depends upon the number of signals to be transmitted per second and upon the nature of the signal.

The usual short-wave receiver for code reception consists of an "autodyne" detector, that is, an oscillating detector which is detuned from the incoming signal by about 1000 cycles. The plate circuit has a low impedance to both the locally generated and the incoming frequency but a high impedance to the 1000-cycle note which is amplified by an ordinary audio amplifier and then passed into a pair of head phones. Frequently a screen-grid tube is used between the detector and the antenna, to provide somewhat greater amplification, to prevent interaction between antenna and detector, and to prevent oscillations in the detector circuit from getting into the antenna and being radiated from it.

Of course it is possible to make the beat frequency between the detector oscillation and the incoming signal some intermediate frequency and to pass it into an intermediate-frequency amplifier. Many of the short-wave "adapters" consist of such apparatus. The intermediate-frequency amplifier can be the usual radio-frequency amplifier from a broadcast receiver. Amplification takes place in such a set at the wavelength to which the broadcast band receiver is tuned, usually about 550 kc.

Other adapters are merely oscillating detectors which are plugged into the detector socket of a broadcast receiver. The tube gets its filament and plate voltage from this socket, and passes its 1000-cycle beat note into the audio amplifier of the broadcast receiver.

293. Short-wave receiver circuits.—The short-wave receiver detector can be made to oscillate in any of the standard regenerative circuits. Since the detector is to work at very high frequencies

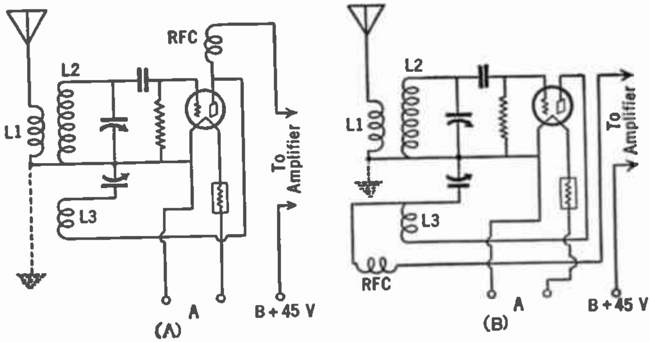


FIG. 217.—Two methods of connecting feed-back circuit in short wave receiver. A preferred circuit is in Fig. 221.

where any stray capacities or shunt paths become of great importance, several circuits have come through the development period to be almost standard, combining ease of adjustment and stability of operation. In Fig. 217 are shown two common circuits. They differ in the manner of securing regeneration. They employ a fixed tickler and a variable capacity adjustment. The variable tickler has been abandoned in short-wave circuits because of variations in tuning when its position is varied with respect to the secondary winding. In Fig. 217*A* the r.-f. currents are prevented from going into the a.-f. amplifier and made to go through the regeneration system by means of the choke coil, *RFC*. If the choke is poor, or if good coupling between tickler and secondary coils cannot be obtained so that regeneration is not under good control, the series arrangement in 217*B* may be used. Here all of the plate circuit currents, a.-f. and r.-f., go through the choke coil. Such a circuit is especially useful if the choke coil does not have a high impedance over the band to be tuned to.

Since the choke coil is directly across the tickler coil and regeneration condenser shown in Fig. 217*A* (the B battery is at ground potential and so is the filament), its low impedance at some frequency may prevent oscillations. This choke coil because of its inductance and capacity will have a resonant frequency, and some harmonic of it may appear within the band to which the receiver may be tuned, or the choke may tune within the band by means of some series capacity. Under these conditions the operation of the receiver will be erratic.

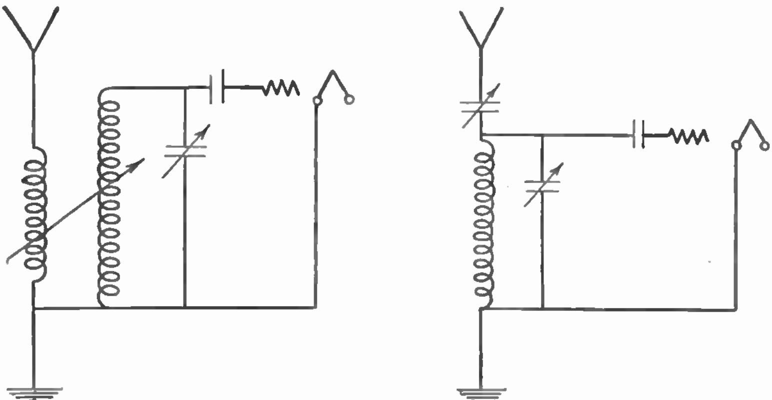


FIG. 218.—Two methods of coupling antenna to input of receiver.

294. Coupling the short-wave receiver to the antenna.—An oscillating tube may be connected directly to the antenna either through a coupling coil or through a small condenser (Fig. 218) or through a coupling tube, usually a screen-grid tube which may or may not be arranged with its input circuit tuned. If the input circuit is tuned, care must be taken to prevent feed-back between its output and this antenna-ground input inductance.

Otherwise the tube and circuit will oscillate, and stable reception will not be possible.

If the antenna is connected either through an inductance or a condenser, some harmonic of the antenna may fall within the band over which the receiver is to be tuned. It will then absorb energy from the oscillating detector and it will be difficult to make the detector regenerate properly. Such difficulties result in " dead spots " and will require a looser coupling to the antenna to prevent interference with the tuning of the receiver. The use of a coupling tube will eliminate dead spots. Its input should be tuned.

295. Use of screen-grid tube at short waves.—Figure 219, taken from the Hammarlund Short Wave Manual, 1929, is the equivalent circuit of the screen-grid tube when used between two impedances, Z_i input and Z_o output. The grid-plate capacity is represented as C_{gp} and the plate resistance of the tube in series with the input voltage multiplied by the μ of the tube is shunted across the circuit. The proportion of voltage usefully employed across Z_o may be found by comparing its impedance to the total impedance of the circuit *DEFG*. If this impedance is 900,000 ohms and if Z_o is 100,000 ohms, the voltage across Z_o will be roughly one-ninth of the voltage developed in the tube, μE_g, and the amplification will be one-ninth of μ, or for the average screen-grid tube about 30. The same result may be calculated by multiplying the mutual conductance of the tube by the output load, $300 \times 10^{-6} \times 100{,}000$. This is because the load, Z_o, is small compared with the R_p of the tube.

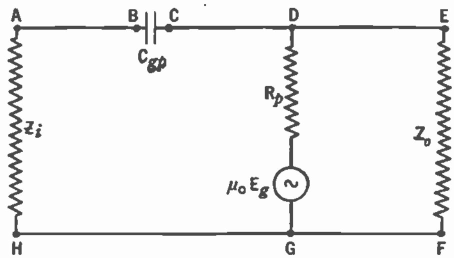


FIG. 219.—Equivalent circuit of screen grid tube and input and output impedances.

At high frequencies the reactance of C_{gp} becomes fairly small and so energy fed into Z_o from the generator, μE_g, may get back to the input circuit, Z_i. This results in regeneration and if this feed-back voltage is equal to the original voltage across AH due the incoming signal, continuous oscillation will probably result. Such a condition is undesirable. If the amplification in the tube is 30, 30 times as much voltage exists across Z_o as across Z_i, and if the reactance of C_{gp} is low enough so that the voltage fed back to Z_i is one-thirtieth of that across Z_o, oscillations result. This will be true when the frequency gets high enough so that the reactance of C_{gp} becomes sufficiently low. If Z_i and Z_o are each equal to about 100,000 ohms, the limiting frequency that can be received with stability is such that the reactance of C_{gp} is 30 times this value or 3,000,000 ohms. Such a frequency is 1770 kc. Frequencies higher than this will cause trouble. One of two things must take place to prevent regeneration: either Z_i or Z_o must be decreased. Decreasing Z_i decreases the proportion of voltage that is fed back, and decreasing Z_o decreases the amplification. If the antenna is connected as in Fig. 220 through a 5000- or 10,000-ohm resistor, trouble from oscillation will not occur. If, on the other hand, the input is tuned (Fig. 221) oscillation may result. The input shown in Fig. 220 is prone to pick up local interference. Fig. 221 is better.

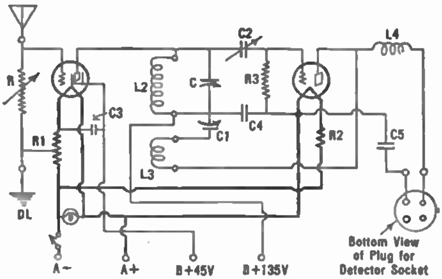


FIG. 220.—A screen grid blocking tube between antenna and oscillating detector; all arranged to be plugged into a broadcast or other receiver.

It becomes a question of extracting the maximum voltage amplification possible from the tube, or from getting less amplification and building up the signal strength by boosting the input voltage to the tube. Tuning the input and keeping the output somewhat low in impedance may result in greater overall amplification than is possible by a low input and high gain. Coupling the screen-grid tube to the detector through rather loose coupling will lower the effective resistance in the plate circuit of this tube and decrease the amplification but increase the stability, and permit a greater input impedance to be built up in the screen-grid stage.

Adjusting the coupling condenser C_x limits the amplification to the value that is stable because the impedance in the plate circuit of the screen-grid tube is low enough to prevent oscillation.

296. Long-wave receivers.—The usual long-wave receiver uses an autodyne detector too, but because of the detuning effect, which may be serious at low frequencies, a better scheme is to use a separate oscillator and to beat it with the incoming signal.

When one listens to long-wave stations for the first time on such simple receivers, he is struck by the fact that many stations are heard at the same time. The reason is as follows. These

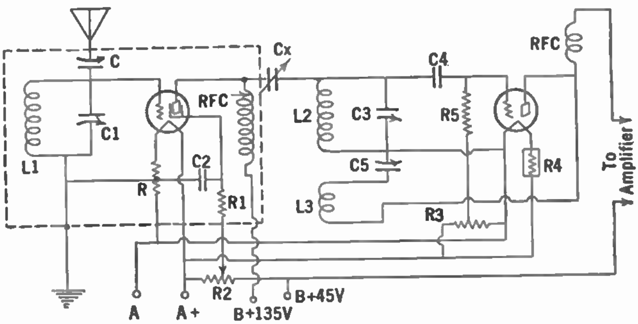


FIG. 221.—A short-wave detector circuit preceded by a tuned amplifier.

stations operate on the frequency band from 10,000 to 20,000 meters or from 15 to 30 kc. When a receiver is tuned to a 20-kc. station, it is detuned only 1000 cycles—an audible amount—from a 21-kc. station, only 2000 cycles from a 22-kc. station, and so on. If the operator tunes to the 10,000-meter—30-kc.—station he is only detuned by 15 kc., an audible amount, from the station allotted the channel at the extreme other end of the band.

In commercial receiving stations the signals are tuned and filtered so that a very narrow band is passed, about 200 cycles. In this manner stations can be separated. All of the long-wave stations in the world are in this limited band, and of course any station can be heard in any other part of the world.

The coils frequently used in receiving high-power long-wave stations are the commonly known "honeycomb" coils and are highly concentrated multi-layer inductances. A table showing the wavelengths to be received with certain sizes of coils is given herewith.

TABLE I

Number of Turns	Inductance, at 800 Cycles, in Millihenrys	Natural Wave-length, Meters	Distributed Capacity in Mmfd.	Wavelength Range, Meters	
				0.0005-mfd. Condenser	0.001-mfd. Condenser
25	.039	65	30	120 to 245	120 to 355
35	.0717	92	33	160 to 335	160 to 480
50	.149	128	31	220 to 485	220 to 690
75	.325	172	26	340 to 715	340 to 1,020
100	.555	218	24	430 to 930	430 to 1,330
150	1.30	282	17	680 to 1,410	680 to 2,060
200	2.31	358	16	900 to 1,880	900 to 2,700
249	3.67	442	15	1,100 to 2,370	1,000 to 3,410
300	5.35	535	17	1,400 to 2,870	1,400 to 4,120
400	9.62	656	13	1,800 to 3,830	1,800 to 5,500
500	15.5	836	13	2,300 to 4,870	2,300 to 2,000
600	21.6	1045	14	2,800 to 5,700	2,800 to 8,200
750	34.2	1300	14	3,500 to 7,200	3,500 to 10,400
1000	61	1700	13	4,700 to 9,600	4,700 to 13,800
1250	102.5	2010	11	6,000 to 12,500	6,000 to 18,000
1500	155	2710	13	7,500 to 15,400	7,500 to 22,100

Experiment 1-15. Connect three honeycomb coils as shown in Fig. 222 making S a 1500-turn coil, P about 1000-turn, and T about 750-turn. The tuning condenser can be either 500 or 1000 mmfd., preferably the latter. Connect an antenna as long as possible to the 750-turn coil and listen in the plate circuit. It may be necessary to reverse the connections to the coil T in order to make the tube oscillate. It should be possible to hear many long-wave stations transmitting traffic to foreign countries. The phenomenon of zero beat is beautifully illustrated by such an experiment. Some of the long-wave stations that should be heard are;

New Brunswick, N. J. . . .	WII	13,750 meters
New Brunswick, N. J. . . .	WRT	13,265 meters
Bolinas, Calif.	KDU	12,500 meters
Rocky Point, N. Y.	WFX	15,806 meters
Rocky Point, N. Y.	WQK	16,465 meters
Rocky Point, N. Y.	WSS	16,120 meters
Tuckerton, N. J.	WCI	16,700 meters
Tuckerton, N. J.	WCG	15,900 meters

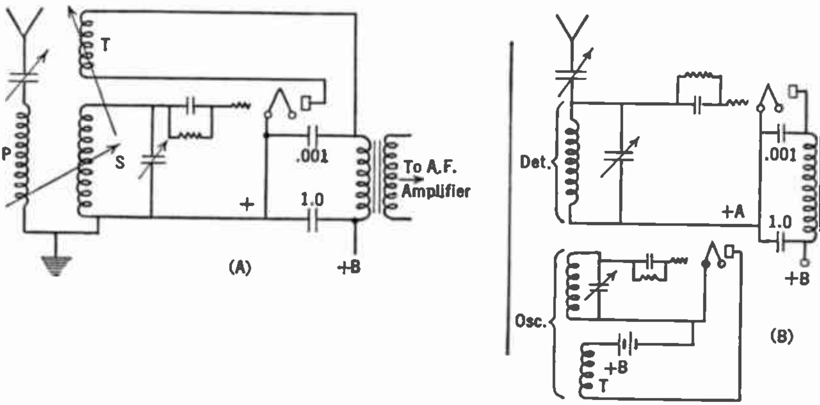


Fig. 222.—The beat note in a code receiver may be obtained in the "autodyne" manner (*A*) or in heterodyne (*B*).

297. Detuning loss in autodynes.—Some loss in signal strength is experienced in autodynes because the detector is actually detuned from the incoming signal. At high frequencies where such a system is frequently used, the detuning is not serious. Thus at 30 meters, 10,000 kc., a deviation of 100,000 cycles is only 1.0 per cent. At the longer waves, however, detuning only 1000 cycles to get an audible beat note represents an appreciable loss. Thus at 20,000 meters, 15 kc., a detuning of 1000 cycles represents a detuning of over 6 per cent. The use of a separate oscillator, as in Fig. 222*B*, will prevent this loss.

Problem 2–15. The following voltages were measured across a 600-turn honeycomb coil when it was tuned to 40 kc. and the input frequency was changed. How much loss in signal strength would be incurred if the coil and condenser were used in an autodyne detector and detuned from 40 kc. so that a 1000-cycle bear note was secured? Plot the curve of voltage against frequency and note the loss from it.

TABLE II

Frequency	Voltage	Frequency	Voltage
38.0	.4	40.0	2.5
38.5	.65	40.5	1.75
39.0	1.05	41.0	.95
39.5	1.75	41.5	.55

298. Poor quality on long waves.—It is much more difficult to transmit or receive high quality music or speech on the longer waves. Suppose the transmitter is tuned to 10,000 meters, 30 kc. The band transmitted must be 10 kc. wide or 30 per cent. At broadcast frequencies, however, the band passed is only 10,000 cycles in a mean frequency of 1000 kc. or 1.0 per cent. This means that very broad circuits must be used at intermediate or low ratio frequencies, which in turn means poorly selective circuits.

299. "Band pass" receivers.—The third type of receiver in common use is due to the desire to provide greater fidelity of reproduction and at the same time to increase the selectivity of the receiver. The ideal response characteristic is a flat-topped curve with very steep sides. Such a curve would provide good transmission within the desired band, say 10,000 cycles, and nothing at all beyond that band. The resonance curve of the ordinary tuned circuit, or of several such circuits in cascade, has a narrow top, and more gently sloping sides than is the ideal.

By the use of coupled circuits it is possible to approach the ideal. Thus in Fig. 223 if both coils are individually tuned to the same frequency, and then coupled together, the resultant response characteristics may be a single narrow-topped curve, like that of a single tuned circuit, or a flat-topped curve, or a curve of two more or less widely separated peaks with a hollow between, depending upon the degree to which the circuits are coupled.

In Fig. 223 is given the result of coupling two such circuits together with various degrees of coupling. It will be seen that too close coupling gives the widely separated peaks, proper coupling gives a comparatively flat-topped characteristic, and too loose coupling gives a sharply tuned circuit, cutting side-bands as badly as a single circuit, although its sides drop more precipitously than

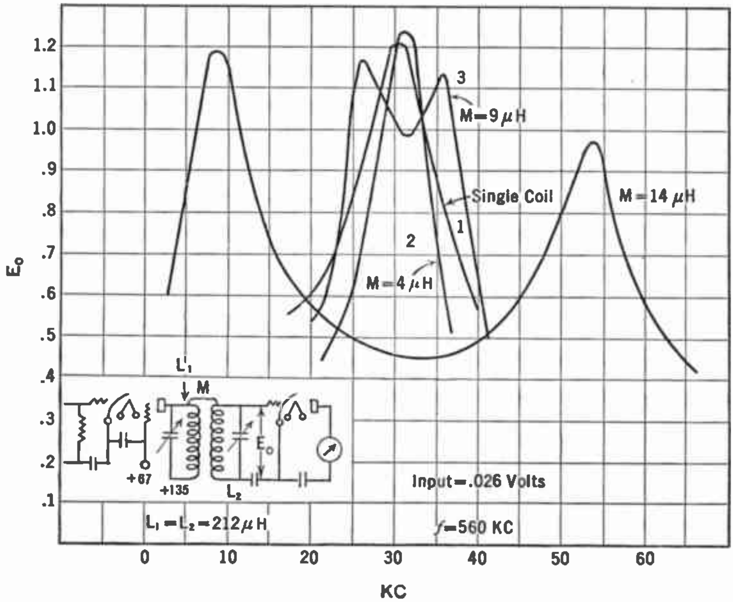


FIG. 223.—Experimental determination of effect of close coupling in band pass filter at high frequencies.

a single circuit and thereby provide greater selectivity against stations at some distance from the resonant frequency.

Superheterodynes now use such a "band pass" circuit in the intermediate frequency amplifier. Here the frequency is fixed, and one adjustment will do for all signals put into it. When the band pass arrangement is used at broadcast frequencies, the width of band passed may differ at each frequency to be received. If the coupling is by inductance the band will be broad at the high frequencies; if the coupling is capacitive, the curve will be broad at low frequencies. Some combination may be arranged so that a more or less uniform band is passed at all broadcast frequencies.

The " band pass " arrangement may be placed between tubes, or several stages of it may be placed ahead of the amplifier, and thus used to filter out the desired band before any amplification takes place. In the latter case an untuned amplifier is necessary, that is, a system which amplifies all frequencies more or less alike.

300. The Sparton receiver.—The first commercial receiver to use the " band pass " arrangement was the Sparton, which had a band selector and an untuned amplifier. The band selector was

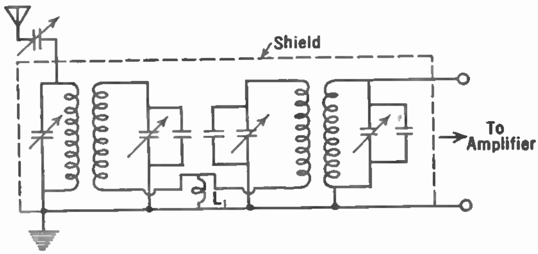


FIG. 224.—Band pass circuit.

composed of several tuned circuits coupled together by means of small inductances as shown in Fig. 224. The amplifier had a voltage gain of about 5000 at 1500 kc. to about 18,000 at 550 kc. In operation the band selector was adjusted so that it admitted and transmitted the desired station's signals. These were amplified by the untuned amplifier, and rectified by the power detector and thence transmitted to the power amplifier.

301. Experiments with band pass filters.—The results of making some laboratory measurements on such filters may be seen in Fig. 225. These data were collected by Kendall Clough and published in *Radio Broadcast*, December, 1928. They show the difficulty in getting a uniform band, or uniform transmission loss or gain, over a wide frequency band. The dotted curves are of a single tuned circuit. The curves show gain in a single stage.

302. Measurements on radio receivers.—It is now possible to make very comprehensive and thoroughly quantitative tests on radio receivers, either as a whole or upon the component parts. Such tests consist in measuring what comes out of a receiver when known voltages at known frequencies modulated at known percentages are placed on the antenna-ground binding posts of the receiver.

The voltage on the antenna-ground posts is secured in several ways. Some laboratories use an artificial or " dummy " antenna

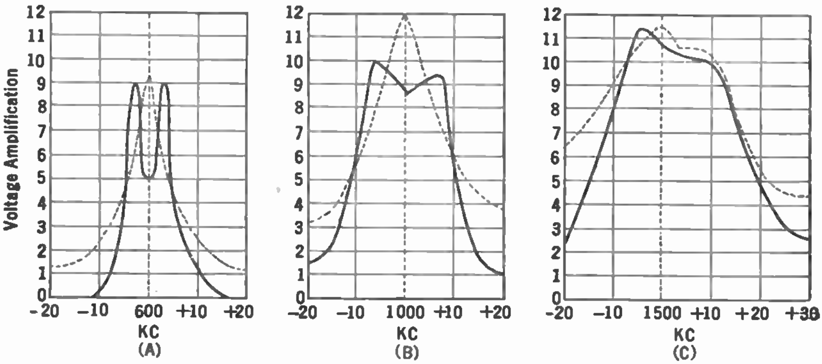


Fig. 225.—Quantitative data on band pass amplifier-tube and tuned coils. The dotted curves are of a single coil properly tuned.

consisting of concentrated capacity and inductance and resistance of such values that they simulate the antenna-ground system ordinarily used. Such values used in some laboratories are: 200 microhenrys, capacity 200 mmfd., and resistance 25 ohms. Other laboratories use a coupling coil into which the desired voltage is induced, and others take the voltage drop across a known resistance which is in series with the artificial antenna. If comparative measurements and not absolute are required, the output from the receiver when it is attached to an antenna of the usual type can be employed. Of two receivers the one which gives more output from a given station on a given antenna has the greater overall amplification. A crystal rectifier and meter will measure output.

The load into which the output of the receiver is measured is usually a non-inductive resistance and the standard output is taken at 50 milliwatts. Sometimes a loud speaker is placed across the receiver output and the current into it and voltage across it are measured with given input voltages and at various frequencies. These volt-amperes plotted against input frequency or against input modulating frequency give an indication of the overall voltage amplification as well as the overall fidelity characteristics of the receiver.

Although it is important to measure the individual components out of which the receiver or power equipment or transmitter is made, the overall characteristic tells the story of exactly what the apparatus as a whole will do.

303. Signal generator.—For receiver measurements some means must be provided for furnishing known amounts of radio-frequency voltages. Since the modern radio receiver has a very high voltage and power amplification, these voltages must be very small when it is desired to measure the overall characteristic or performance. It is desirable to have a known voltage at least as low as 1 microvolt, and anyone who has worked intimately with radio-frequency voltages—at one million cycles for example, knows how difficult it is to know when one has an e.m.f. of this order or a current of one millionth of an ampere. The laboratory worker must know how much current or voltage he has, and he must be certain that his meter shows all the current or voltage, no more and no less.

The circuit diagram in Fig. 226 is that of the General Radio Signal Generator, a device which consists of a radio-frequency oscillator, a means of measuring and controlling its ouput, and a means of using any desired part of this output for purposes of measuring receivers, either as a whole or in component parts.

In practice a fairly large current is measured, which flows through a known resistance and provides a fairly large voltage. Then an " attenuator " or voltage decreasing system is provided which has been calibrated, preferably in DB, so that any desired known part of this fairly large voltage can be presented to some outside circuit.

304. Modern receivers.—Some sensitivity and selectivity curves of a modern receiver (Stromberg Carlson Model 641) will

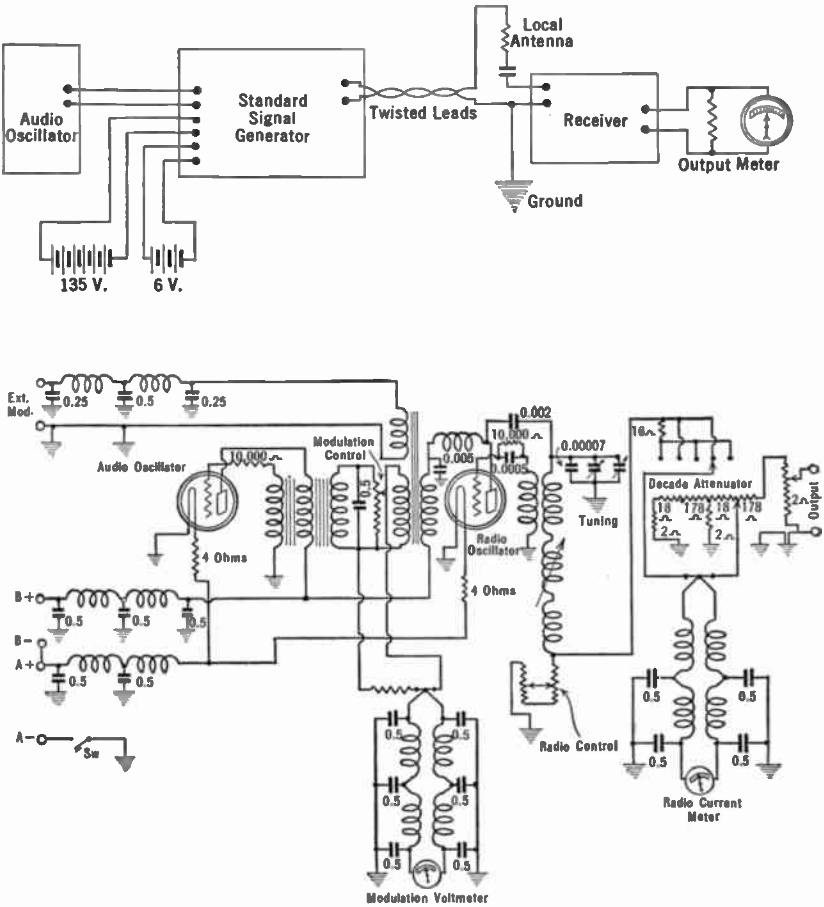


FIG. 226.—Circuit diagram and method of using signal generator.

be found in Figs. 227 and 228. They are characteristic of the better sets made in 1928–1929. Such receivers are more sensitive than is necessary and probably would not be made to deliver a normal output on such low field strengths were it not for competition and the lure of " Dx."

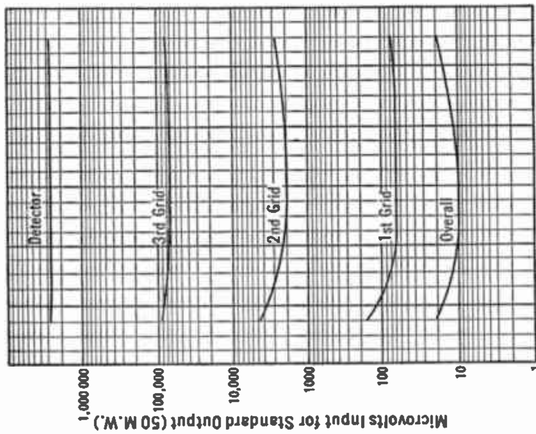


FIG. 227.—Sensitivity curves of 1929 receiver (Stromberg-Carlson Model 641).

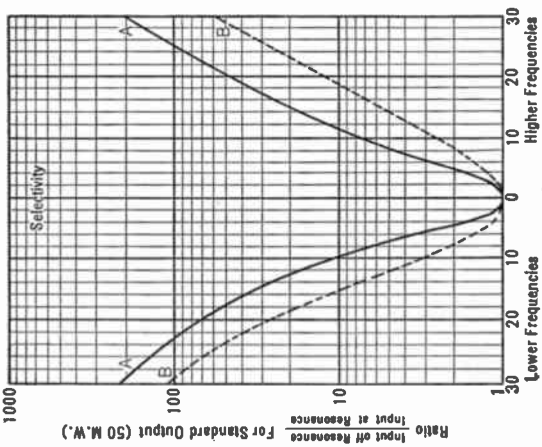


FIG. 228.—Selectivity curve of 1929 receiver, *A* compared to 1928, *B*.

Screen-grid tubes make possible receivers with fewer tubes, greater sensitivity, greater selectivity, and perhaps better fidelity. Two screen-grid tubes should deliver a voltage amplification at average broadcast frequencies of 2500 and if there is a voltage gain of 5 in the antenna or another stage of amplification tremendous voltage amplification becomes possible. Just what can be done with such amplification is a question. In most cities the noise level is so high that a receiver probably can never utilize its full amplification.

The possibility of enormous amplification preceding the detector eliminates considerable distortion occurring in weak signal detectors by working them at higher levels where linear detection takes place, removes some hum from the output, and considerable audio-frequency regeneration. At the same time the screen-grid tubes make possible a more selective receiver (their resistance is very high and can be shunted across tuned circuits without increasing the resistance of the latter so much as when 12,000-ohm tubes are employed) and such selectivity may imply that some high audio tones are cut out. To get around this difficulty manufacturers are experimenting with band pass tuning which, theoretically at least, presents a flat-dopped, steep-sided resonance curve.

305. Apparent and real selectivity.—The fact that the sensitivity and selectivity of a receiver are interrelated has been mentioned. Even in those few receivers in which the two functions are separated, there is an apparent relation between these two important factors. The more sensitive a receiver is the less selective it seems to be. This is because the more sensitive it is, the more it amplifies weak signals. On a less sensitive receiver, signals on a frequency channel near the one to which the set is tuned may be so weak they do not bother the desired program. If the sensitivity of the receiver is increased, the desired signal increases in level but so does the unwanted signal. Both may increase in the same ratio, so that the real or measurable selectivity remains the same, but the unwanted station now begins to affect the listener's ear. When the desired station is quiet, during announcements for example, the unwanted station comes in.

The answer is to decrease the sensitivity of the receiver so that the unwanted signal is again pressed below the level (*A* in Fig. 229) where it is bothersome, and if more volume is required to increase the audio-frequency amplification. Thus a receiver should have a sensistivity control and a volume control. The first operates on the radio-frequency amplifier, the latter may operate on either the radio- or the audio-frequency amplifier. In Fig. 229 the vertical lines represent broadcasting signals. In *B*, three of them are being received, the 1000 kc. the loudest. In *A* only one signal, at 1000 kc. is entering the receiver.

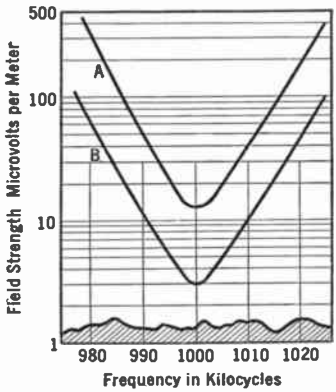


FIG. 229.—Illustrating real and apparent selectivity.

306. Importance of shape of condenser plates.—A receiver can be calibrated so that each degree of its dial may represent one channel width, 10 kc., or it may be calibrated in wavelengths so that turning the dial a certain number of degrees turns through a certain number of meters. Or a combination of "straight frequency line" and "straight wavelength line" tuning may be effected. With a semicircular plate condenser a greater number of frequency channels, each 10 kc. wide, will be passed over by a given number of dial degrees at the high frequencies than at the low, and the effect upon the operator is an apparent decrease in selectivity of his receiver at short wavelengths.

307. Automatic tuning.—Several schemes have been proposed for automatically tuning a receiver; some of them have been patented and utilized in commercial models of receivers. Such a receiver has a switch or a button, or a lever, on which is marked the station desired. It is only necessary to operate the device to tune the receiver to the desired frequency. Pressing another button tunes in another station.

Such systems can be operated with electrical relays, one relay setting the circuits for each frequency, or by mechanical devices, levers, motors, etc.

308. Automatic volume control.—Some advance has been made toward automatic volume control for radio receivers. Anyone who has operated a receiver at such a distance from the transmitter that fading is pronounced will appreciate the need for such circuits. The use of such a volume control means that once the adjustment for maximum sound output has been made, tuning the receiver through local and distant stations will not produce blasts of distorted sounds when passing the carrier wave of a strong station. Provided the distant station puts down a sufficient field strength near the receiver, it can be brought in with the same volume as a local station. The difference in the majority of cases will be in the noise that comes along with the station's signals. That is, if the distant station is much weaker than the local station, the sensitivity of the receiver will be increased automatically by the control system to the point where the distant station gives loud speaker signals. In this sensitive condition the receiver will admit other extraneous radio-frequency disturbances, such as static, power leaks, etc.

One volume-control circuit is shown in Fig. 230 and is applied to the Radiola 64. It is simply a tube placed in parallel with the second detector of the receiver. When loud signals are received this tube has its grid voltage decreased and hence its plate current increased. This increased plate current produces a voltage drop across a resistance and is then applied to the grids of the radio- and intermediate-frequency amplifier tubes thereby increasing the negative bias and reducing the overall amplification. Some manual adjustment is provided so that the output level at which the volume control begins to work is under control of the operator.

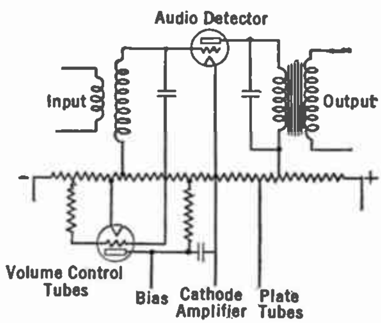


FIG. 230.—Automatic volume control circuit.

309. Shielded receivers.—The greater the voltage gain in a radio-frequency amplifier, the more necessary it is to prevent any energy from a tube near the detector from feeding back into a tube near the antenna. Otherwise oscillation results and the receiver is useless. One method is to neutralize the grid-plate capacity within the tube. Another is to filter each plate and grid lead so that the r.-f. currents stay where they belong and do not get into the plate voltage supply system. Still another is shielding.

Now placing a coil in a metal box seems like a simple trick to keep the lines of force from that coil from getting mixed up with lines of force from another coil. But the size of the metal box, its material, the size of the coil, whether or not the metal box is grounded, and to what, and whether it carries current or not—all of these things enter into the problem of shielding.

If the lines of force from a coil are stopped by the shield, currents are set up in this metallic shield. These currents, flowing through the resistance of the shield, represent a certain amount of power lost. This power must be supplied from the tuned circuit, and is thereby subtracted from the useful function of providing signal strength to actuate the grid of some succeeding tube.

The subtraction of energy from the tuned circuit by the shield has the same effect as though the resistance of the tuned circuit were increased. In other words, if currents are induced in the shield, the effective resistance of the coil is increased, its selectivity factor goes down, the voltage gain due the coil and condenser is decreased. It is also true that the inductance of the coil decreases too, so that the value of effective resistance for the tuned circuit, $L^2\omega^2/r$ is greatly decreased. The nearer the coil is to the shield, and the greater the resistance of the shield, the greater is the power loss in it. If the shield is made up of sections which slide into each other and these sections do not fit tightly, a joint of high resistance may result. This means that not only is the shield ineffective but that it consumes too much useful energy from the tuned circuit. The shield must be large compared to the coil.

The shield should never be used to carry current. That is, attaching a filament wire to one end and the battery to another is bad practice. It is still worse practice to make it a part of any tuned circuit. The shield should be made heavy and from the best conductor economically possible, and all joints in it should be carefully soldered. It should be connected at only one point to a heavy conductor leading to the common ground of the set. Holes in it for leading-in or -out wires should be small.

From the electrical standpoint, copper is better than brass or aluminum; from the standpoint of weight and cost per pound, copper is handicapped.

It is interesting to consider the circuit as a transformer and its load. The resistance of the shield represents the load across the transformer. The power in this load is taken from the generator which is the tuned circuit. As a matter of fact any two wires which couple any two circuits together may be considered as a transformer, one acting as the primary and the other as the secondary. The power wasted in the load on the secondary wire must come from the generator or the circuit attached to the primary wire and represents an increase in the resistance of the circuit attached to this wire, and a decrease in its inductance.

310. Loud speakers.—The loud speaker is the final link in the broadcasting system, and because of its position with respect to the listener it is frequently blamed for much of the bad reproduction that really originates somewhere else.

The task of the loud speaker is to translate into sound energy the electrical energy in the power tube. It must do this as effectively and faithfully as possible. It is useless to design and operate a high-class amplifier with a poor loud speaker. The wide range of tones coming from the amplifier is lost in the loud speaker and does not get to the listener. Likewise, it is absurd to install a perfect loud speaker in the hope that the fidelity of reproduction from an antiquated or poorly engineered receiver will be bettered. The full benefit of a perfect loud speaker cannot be attained until the complete chain of apparatus is perfect—amplifier, power tube, plate voltage supply, loud speaker, etc.

Loud speakers in general are notoriously inefficient—the best in common use is not over 30 per cent. Most of them are less than 5 per cent efficient. Some of them reproduce the whole audio range of tones with almost equal fidelity. Others reproduce only a very small section of the audio spectrum—such were the short-horned loud speakers of a few years ago.

311. The horn type.—Any device which will move when a modulated electric current flows in it will make a loud speaker. Its movements are imparted to the air which in turn affect our ear drums and our auditory nerves in a sensation we call sound. The object is to effect as large a movement of air as possible with the least possible electrical input, and to effect this efficient transfer of electrical into sound energy over as wide a band of audio tones as possible.

The horn type of speaker may use a thin steel or iron diaphragm as the moving element or a non-magnetic diaphragm actuated by a mechanical coupling system as in Fig. 231. The electric currents are sent through the winding of a nearby electromagnet which has a certain amount of permanent magnetism in it. When the electric currents change the latter's magnetism, the diaphragm or the armature is moved accordingly. These movements are imparted to the air.

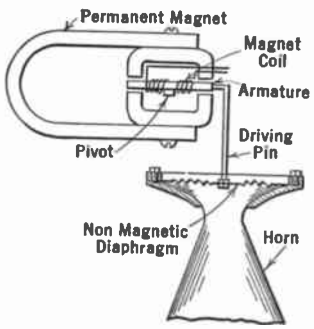


FIG. 231.—Horn type speaker mechanism.

If the horn is large enough the resonance effect of the diaphragm may be partially eliminated. Otherwise when the frequency at which this diaphragm mechanically resonates comes through the speaker windings, a very loud output will be given out showing that the loud speaker element is more efficient at this particular frequency. The horn acts as a load upon the diaphragm much as a resistance across the secondary of a transformer acts as a load on a generator connected to the primary which supplies the power. The power in this case is sound power radiated from the horn. Very long horns which expand from a small opening near the diaphragm to a very wide mouth in an "exponential" manner give the best response characteristic, in that they are freest from resonances.

If the horn is replaced by a cone, as shown in Fig. 232, much better frequency response results because the cone has a larger area and can give appreciable sound output at low frequencies. With a given diaphragm area, halving the frequency requires four times the relative motion of the diaphragm to produce the same sound power, while increasing the size of the cone so that much greater areas of air are displaced with a given amount of diaphragm (cone) motion, enables lower frequencies to be reproduced.

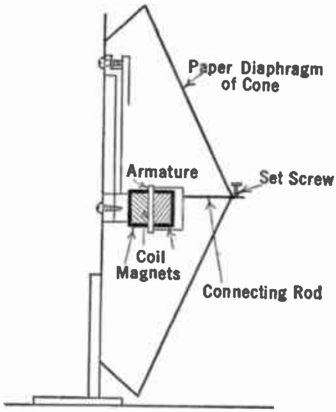


FIG. 232.—Cone type speaker.

Such speakers have an impedance that increases with frequency, being about 1000 ohms at 100 cycles and running as high as 40,000 ohms at 5000 cycles. This means that the tube works into a constantly varying impedance as the frequency varies, and that most efficient transfer of energy, or transfer with least distortion, can occur at only a small range of frequencies. Owing to the fact that the impedance is low at low frequencies, more distortion due to curvature of the tube characteristic takes place at this end of the audio band. It is a fact that such speakers have a very limited motion so that it is impossible to transmit very large low-frequency responses to them, and so the distortion due to curvature is not so pronounced as theory would indicate. For average home use, a good cone speaker about 2 feet in diameter will satisfy the vast majority of listeners.

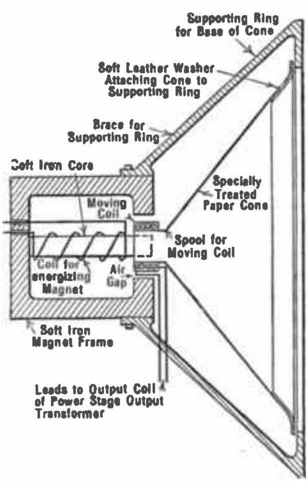


FIG. 233.—Modern "dynamic" or moving coil loud speaker.

312. The moving coil speaker.—The construction of the moving coil or dynamic type of speaker is shown in Fig. 233. A strong magnet is energized by a direct current, either from a storage battery, or from part of the plate current supply system, or from the 110-volt a.-c. line by means of a rectifier. The voice frequency currents coming from the final power tube in the amplifier are passed through a few turns around a small movable coil to which is attached the diaphragm, or cone. When a.-c. currents flow through the coil, it tends to move at right angles to the lines of force across the air gap. These motions of the coil are imparted to the cone and thence to the air.

The impedance of this movable coil is very low, of the order of 5 to 10 ohms, and is almost constant at audio frequencies. This means that the tube looks into its own impedance through a step-down transformer. For this reason a much flatter response curve is possible. Because the coil can move through a considerable distance without danger of any mechanical noises—such as caused by the diaphragm rattling against the poles of a unit of the type of Fig. 231—much better low-frequency response is possible. Considerable sound energy can be got from such a speaker. The resonant frequency of the moving part is usually lower than the lowest audio tone to be reproduced.

313. Baffles for dynamic speakers.—It is necessary to install such a speaker in the center of a rather large and heavy " baffle " if the low notes are to be properly reproduced. Otherwise the wave set up from the back of the cone can interfere with the wave set up by the front with the result that little or no sound gets to the listener. The baffle increases the air path between front and back and should be great enough so that the shortest mechanical path between front and back edges is at least one-quarter wavelength for the shortest lowest note to be received. Since the wavelength of sound, like that of radio waves, is equal to the velocity it travels divided by the frequency, it is not difficult to prove that a baffle at least 32 inches square is necessary for notes as low as 100 cycles, and 110 inches for notes as low as 30 cycles. When the unit is mounted in a box, peculiar resonances are set up which spoil the good qualities of the moving coil speaker.

The turns ratio of the input transformer is about 25 to 1 with conventional speakers and tubes.

314. The electrostatic loud speaker.—The sound output in a moving coil speaker is due to current variations in a coil of wire. In the electrostatic speaker, sounds are set up by changes in voltage on two plates which are insulated from each other. In other words an electrostatic speaker is a condenser consisting of two insulated plates maintained at a high potential difference with respect to each other. Across the plates are added the changing potentials coming from the last amplifier tube. These changing potentials cause a motion of one plate of the speaker with respect to the other and thereby set up sound waves.

In practice a small receiving tube is used as a rectifier supplying from 200 to 600 volts of partially rectified d.c. to the plate of the speaker. The current requirements are very small, thus a small tube may give long life. The variations in voltage are fed to the speaker through an output transformer.

315. The telephone receiver.—Long before the day of the loud speaker, the pair of head phones which could be strapped to an operator's ears was the translator of electric currents into sound waves. Such a device consisted of a permanent magnet and a coil of wire wound about one or both of the poles of the magnet. A diaphragm was placed in the permanent field of the fixed magnet, and also in the field of the coil through which the changing electric currents passed. Why is the permanent magnet necessary?

Consider only the coil through which the a.-c. currents flow, and the diaphragm. Any current flowing through the coil regardless of its direction would attract the iron diaphragm. If, then, a sine wave at 500 cycles were put through the coil 1000 times a second there would be a maximum of current through the coil, and the diaphragm would be attracted toward it this many times, each time being pulled back to its original position by a spring or by its own resilience. In other words, a 500-cycle note would sound to the listener like 1000 cycles; all frequencies put into the receiver or head phones would be doubled in pitch.

This causes no great difficulty in code reception, but in voice reception it would be strange indeed. If, however, the diaphragm is always under some mechanical tension by being near a strong permanent magnet, then smaller variations in magnetism, due to changing a.-c. current, would cause the diaphragm to fluctuate about this permanent pull as an a.-f. average. Then when the a.-c. current was in such a direction that it aided the permanent magnet, the diaphragm would be pulled nearer the pole piece; on the

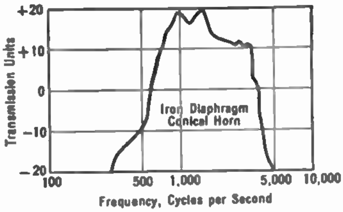


Fig. 234.—Limited response of horn speaker.

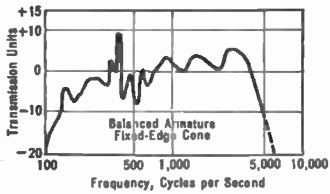


Fig. 235.—Response characteristic of good cone.

other half-cycles when the a.-c. current was in such a direction that it opposed or weakened the permanent field, the diaphragm would be released from its mean or average position. The diaphragm, then, would reproduce the exact tone, and not double it.

316. Loud speaker measurements.—It is not difficult to measure the performance of a loud speaker. The procedure is to hang a

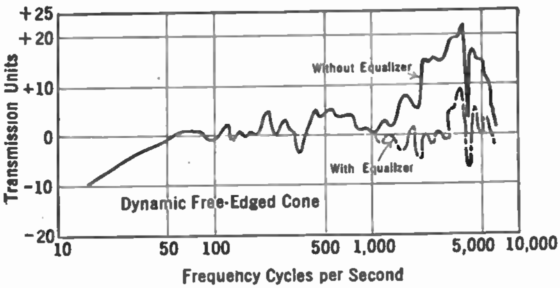


Fig. 236.—Wide range of tones covered by dynamic speaker.

calibrated microphone in front of the speaker which is actuated by various tones of known amplitudes from an oscillator. The output of the microphone is amplified and measured, and thus a curve of output versus frequency may be obtained. Such curves are shown in Figs. 234, 235, and 236.

Dynamic type speakers have a tendency to deliver more output at high frequencies where the cone ceases acting as a plunger and begins to act merely as a small cone. An electric filter consisting of inductance, capacity, and resistance may be put across the speaker to absorb this greater output and keep it from bothering the listener. If, for example, the frequency is about 4000 cycles, as in Fig. 236, a condenser in series with resistance and inductance may be tuned to this frequency and placed across the loud speaker. At all other frequencies it will be merely a high shunting path and take no power. But at 4000 cycles its impedance is low, and currents of this frequency go through it instead of the speaker. The resistance is used to keep the filter from being too sharply tuned.

Similar filters are used in phonograph reproduction to eliminate the needle noise. They are called scratch filters and may tune somewhere between 3000 and 5000 cycles. Of course such filters take out their share of the desired signals and may make the records sound " boomy " which is an indication of too much bass for the amount of high notes.

CHAPTER XVI

RECTIFIERS AND POWER SUPPLY APPARATUS

TUBES which distort may act as rectifiers to transform a.-c. currents into d.-c. currents and thereby be useful as sources of unidirectional current either for charging batteries or for supplying plate voltages to a receiver or other device. Such tubes have only two elements, the source of electrons and the plate or receiver of electrons.

317. The fundamental rectifier circuit.—When such a two-element tube filament is heated to a proper temperature electrons will flow to the plate provided it is at a higher positive potential than the filament. If an a.-c. voltage is connected between the filament and the plate (Fig. 237) an electron current will flow to the plate when the latter is positive and not when it is negative. In other words current flows on the halves of the cycle when the plate is positive; on the halves of the cycle when the plate is negative, the electrons return to the filament as fast as they escape. The a.-c. voltage may be introduced into the plate-filament path by means of a transformer, which also supplies the heating current for the filaments as shown in Fig. 238.

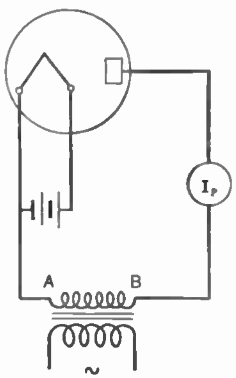


FIG. 237.—Fundamental rectifier circuit.

A d.-c. meter in the plate circuit would read a certain amount of current which would be a value somewhere between the maximum current that flowed during each positive half-cycle, and zero. The meter needle would not follow the rapid spurts of current and so would assume some average value. If we consider as the input the a.-c. voltage, and the d.-c. meter as the output circuit, it is clear that distortion is taking place, because there is no d.-c. in the input and there is a readable amount of d.c. appearing in the output. In other words the output is not a perfect replica of the input.

Such a rectifier may be arranged to transform a.c. to pulsating d.c. either at low, medium, or very high voltages. Whenever one wants a source of d.c. voltage or current and an a.-c. voltage only is available, a vacuum tube operating as a rectifier may be employed.

Rectification takes place only in this one direction. It is not a reversible process. If we want a.c. from d.c. we must use a motor-generator, a converter, or a vacuum tube which can be made to oscillate and thereby convert a certain amount of d.-c. power from batteries into a.-c. power.

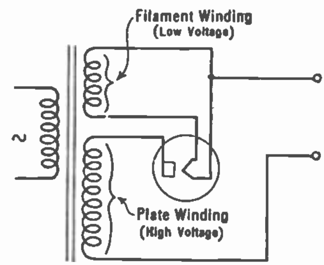


FIG. 238.—Operating rectifier filament from a. c.

The amount of d.-c. current that would be read by a meter in the plate circuit of such a tube would depend upon the voltage, the form of the wave being rectified, the shape of the tube characteristic, the amount of current that flows when the plate is negative with respect to the filament, and upon other factors. If one could listen to the output of such a tube, as one may by putting a loud speaker in series with it, he would hear a buzzing or throbbing sound.

The a.-c. voltage input wave is as in *A*, Fig. 239, which shows the output without a rectifier. The pulses of d.-c. in the plate circuit of a single wave rectifier are as in *B*. This is not a direct current in the ordinary sense of the expression. It is a current which varies in amplitude over the half-cycle of the a.-c. voltage which makes the plate positive. The current throughout this half-cycle flows in the same direction, however, and so may be considered as a pulsating direct current. These pulsations may be smoothed out by filters and as a result nearly pure uni-directional constant amplitude d.-c. current may be obtained.

318. Kinds of rectifiers.—A rectifier, then, is a device which transforms a.-c. current into a pulsating current which can be smoothed out into pure d.-c. current if desired. Rectification may take place (*a*) in a device which passes more current in one direction than it does in another, or (*b*) in a device which does not pass any current at all in one direction, or (*c*) in a device which passes

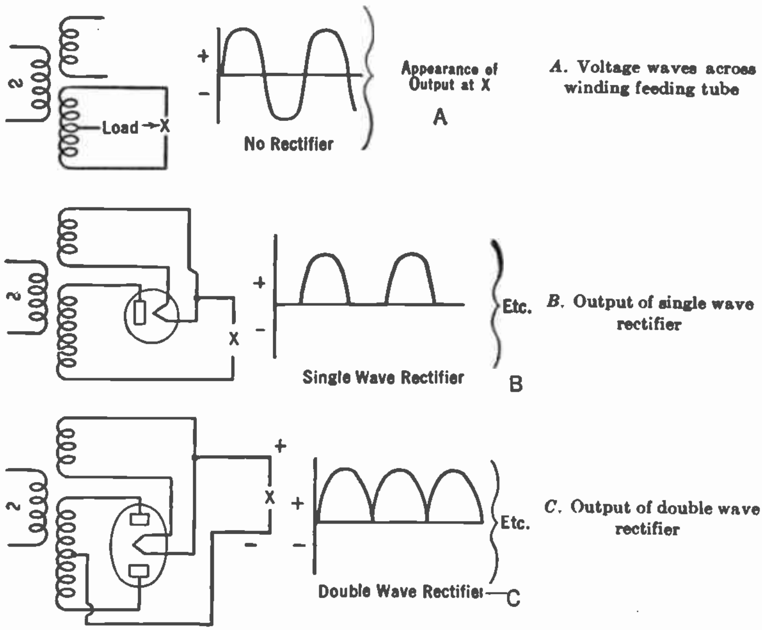


FIG. 239.

current when the voltage is increased beyond a certain limiting value, but no current below that value or in the opposite direction.

If the plate of a rectifier tube is kept cool, so that it cannot act as a source of electrons, the tube will pass no current when the plate is negative with respect to the filament and the two-element tube rectifier then is a member of class (*b*) above. If, however, a large amount of rectified current is permitted to flow through a fairly high resistance tube the plate may become hot, and so act as a source of electrons on the half-cycle when the plate is negative with respect to the filament, and some " back " current will flow. The tube then falls into class (*a*). Such a condition in a modern plate voltage supply system is not likely to occur and will be evidenced by a high degree of hum in the output of the receiver.

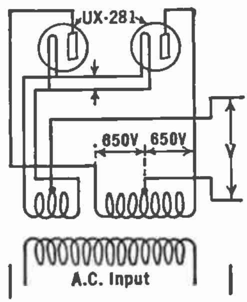


FIG. 240.—Connections of a full wave rectifier.

Certain crystals, such as galena, silicon, or silicon carbon (trade name " carborundum "), etc., are rectifiers, passing more current in one direction than they do in another and fall into class (*a*). Some tubes do not use a filament, but have in them a gas, neon or helium for example, which ionizes when the voltage reaches a certain value and conducts current in a definite direction. They are members of class (*c*) and will be described below.

The more perfect the rectification the greater will be the d.-c. output from a given a.-c. input. If the rectifier is perfect and if the input is a sine wave, a d.-c. meter in a resistance load will read 0.901 times the a.-c. input current. If 1 ampere a.c. flows in, 0.901 ampere d.c. flows out.

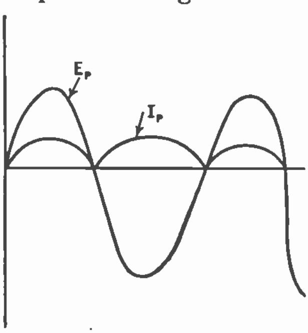


FIG. 241.—Current from a double- or full-wave rectifier to the form approximated by I_p.

319. Typical filament rectifiers.—Tubes used primarily for rectifiers have only two elements, the plate and the filament. They are of two kinds, the single or half-wave rectifier, and the double or full-wave rectifier. The single-wave rectifier has a single filament and a single plate and rectification takes place in it according to the process described above. If desired two such tubes may be arranged, as in Fig. 240, so that each half of the a.-c. cycle is rectified, and so the output current would look like Fig. 241.

A single-tube rectifier which operates on only half the a.-c.

cycle is called a half-wave or single-wave rectifier. The two-tube rectifier is called a full- or double-wave rectifier. It is possible to combine both the single-wave rectifier tubes into one glass container by using two filaments in series and two plates. In such a case full-wave rectification takes place with the use of only one tube. The 280 is such a tube. It has two filaments and two plates and is connected as in Fig. 239*C*.

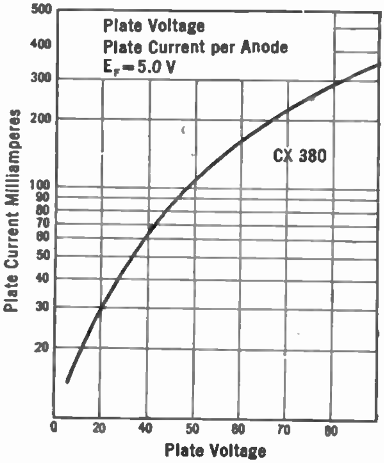


Fig. 242.—Characteristic of double wave rectifier tube.

Characteristic curves of single- and full-wave rectifiers are shown in Figs. 242 and 243.

320. Requirements for rectifier tubes.—The filament of a rectifier tube must be rugged and capable of supplying many more electrons than are ever needed for the proper operation of the output circuit. Thus if a tube is to supply 125 milliamperes steadily, it is possible that in some circuits the instantaneous current through the tube may be as high as 300 milliamperes and the tube must be able to supply this current without saturating. If the tube saturates, the pulse of current when the plate is positive will be difficult to filter, and the rectifier and circuit would suffer from other faults.

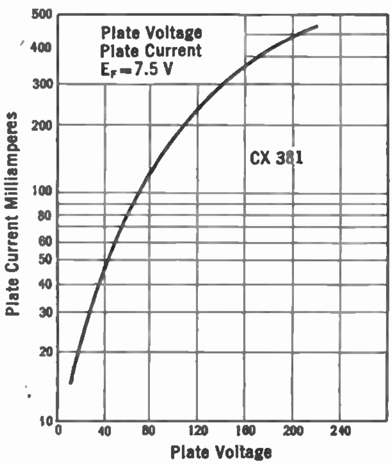


Fig. 243.—Single wave rectifier tube characteristic.

The resistance of the tube should be low so that no great amount of voltage is lost in it, and so that the " regulation " of the

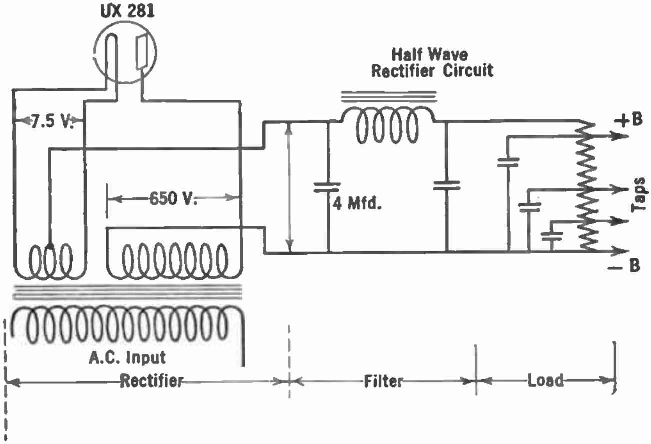


FIG. 244.—Circuit of single wave rectifier, filter and load.

rectifier and filter may be good. A low-resistance tube of course wastes less power, and so less heat must be dissipated. The insulation between filament and plate must be such that breakdown cannot occur either due to direct puncture of some part of the tube or to heating due to leakage currents.

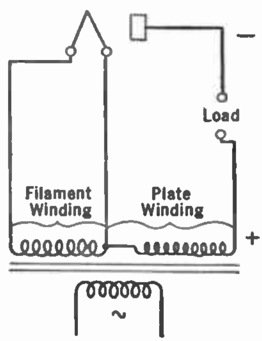


FIG. 245.—Single wave rectifier circuit employed by some Western Electric systems.

321. Single-wave rectifier.—Typical single-wave rectifier circuits are shown in Figs. 244 and 245. The only difference between these circuits lies in the manner in which the load is connected to the circuit, that is, whether it goes next to the plate or next the filament of the rectifier tube. In Fig. 245 the plate of the tube is near ground potential but the transformer is " hot." In the other case, Fig. 244—which is more generally used—the transformer is nearest the ground potential while the tube has a high potential across it. Considering Fig. 244 when the plate end of the secondary or high-voltage winding of the transformer is positive, the other end of the secondary winding is negative with respect to the plate end and a large voltage exists across it—perhaps 400 or 500 volts. This makes the end of the load attached to this end of the transformer negative; and as we proceed in this direction, through the load and back to the filament of the tube, the circuit becomes more and more positive. The filament of a rectifier, then, is the positive end of the circuit so far as the load is concerned. The plate end is the negative or grounded end so far as the load is concerned, and a voltmeter across the load must be connected with this polarity in mind.

When the polarity reverses, on the other half-cycle, the plate end of the transformer becomes negative and the filament end positive. No current flows through the load or tube then, because the plate cannot attract electrons to it from the filament. The device is a half-wave rectifier only. It rectifies half the time. When current flows, the voltage drop across the tube is only the *IR* drop there—not the full transformer voltage.

Now suppose we connect another transformer secondary and another tube as in Fig. 246. When the plate terminal of S_1 attached to the plate of tube 1 is positive, current flows through that tube and returns to the center of the transformer. Nothing happens in tube 2 because the plate of this tube is negative. When the direction of the a.-c. voltage reverses, the plate of tube 2 becomes positive and current flows through this tube returning through the center of the secondary winding as before. Current flows in a given direction through the load resistance regardless of which tube is passing current.

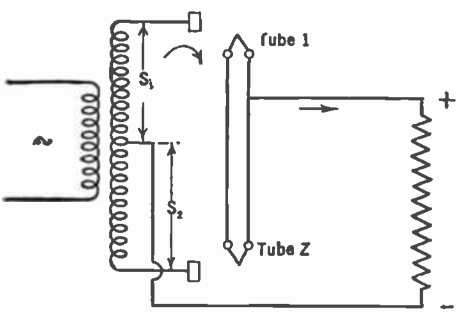


FIG. 246.—Direction of flow of current in full wave rectifier.

322. Gaseous rectifiers.—An important rectifier is the Raytheon tube. It was the first really useful rectifier brought to public use. It is a gaseous double-wave rectifier. The Raytheon tube has undergone several improvements since 1925 when it was first brought out and has been installed in many hundred thousand plate voltage supply devices. It is one of the single most important devices in the history of broadcasting.

The theory of the Raytheon tube is interesting. It employs no filament, and therefore is not an electron discharge tube. To understand its action we must go back again to the electron theory.

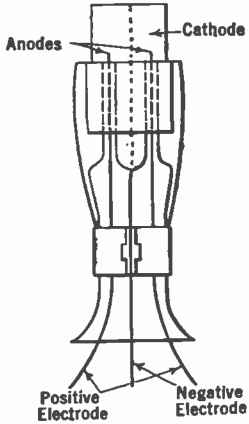


FIG. 247.—Raytheon tube construction.

Within the glass wall of the tube is an inert gas, that is, a gas which, like argon, helium, neon, etc., does not combine chemically with other elements. The molecules and atoms of this gas are neutral electrically, having neither a surplus nor lack of electrons. There are, of course, a few free electrons floating about within the glass container, or a few may be removed from one of the elements when a voltage is placed on it. The elements in a sinlge-wave rectifier are two: first, a narrow strip or pillar of metal, and second, a larger envelope or plate of metal. If the tube is to be a full-wave rectifier, two strips are necessary. They are shown in Fig. 247.

Let us for the moment neglect the gas and consider a stray electron that may be between the narrow and the large electrode. Let us consider the moment when an a.-c. voltage on the two electrodes makes the narrow electrode negative and the large plate positive. The electron will be attracted toward the large plate and will get greater and greater velocity the nearer it approaches the plate. Since the large plate has considerable area it can take care of all of the electrons that may be attracted to it. On the other half-cycle the small electrode becomes positive, but because of its limited area can take care of only a few electrons. The current transported by these electrons is large in one direction, and small in another, thus making the tube a rectifier falling into class (*b*) of Section 318.

If the tube is well pumped and if the electrodes are properly placed there will be little or no current flowing even though the voltage applied to the tube may be considerable. Now let us put some gas in the tube, helium for example. When an electron finds itself in the field between the two electrodes it is attracted toward the positive and gets up greater and greater speed as it progresses. If the distance and the potential difference between electrodes is great enough, the electron may get up enough speed that when, and if, it hits a gas molecule it may knock another electron out of the molecule. This makes two electrons instead of one and of course when they finally arrive at the positive plate they deliver twice as much electricity as if only one were present. As a matter of fact, when the second electron is knocked out of the gas molecule it starts gathering speed, and before it reaches the positive electrode may come in contact with another molecule and release another electron. The process is cumulative, the more electrons the greater the number of collisions per second, and the greater the current carried across the space.

Now when the small electrode is positive, only a few electrons can come into contact with it, and thereby give up their quota of electricity, and the current during this half-cycle is small. The swarm of electrons in the space between the two electrodes tends to keep the current small because of the space charge effect.

There are two necessary features in this tube. There must be gas which can be " ionized " by the electron collisions, and there must be sufficient distance between the two electrodes for the electron speed to become great enough to dislodge additional electricity carriers. The voltage across the tube must be sufficient to impart this speed to the electrons, and on one half-cycle there must be some restriction to the number of electrons per second that can arrive at the positive plate.

323. Characteristics of gaseous rectifiers.—The output of such rectifiers is somewhat more difficult to filter than when an electron flow tube is used because there is some back current, that is, current which flows when the small electrode is positive. On the whole the popularity of the gaseous rectifier tube has been not misplaced. A typical Raytheon rectifier and filter assembly is shown in Fig. 248. It differs from filament type circuits in the addition of two small condensers across the two halves of the transformer secondary; they are known as " buffer " condensers and usually are of 0.1 mfd.

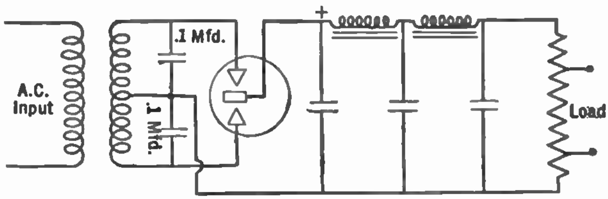


FIG. 248.—Raytheon rectifier circuit.

capacity although more recent tubes require only about .01 mfd. They eliminate any radio-frequency disturbances set up in the circuit due to the abrupt manner in which the rectified current starts and stops.

The Raytheon BH type has a rating of 125 milliamperes.

324. The Tungar rectifier.—The Tungar rectifier introduced in 1916 is a low-voltage, high-current tube of the combined gaseous and filament type. It is designed to rectify a.-c. current into a form suitable for charging batteries, and as a matter of fact was used to supply current for the filament circuits of some early models of a.-c.-operated radio receivers. Its starting or breakdown voltage is about 15 volts and useful life about 2000 hours. The gas is usually argon.

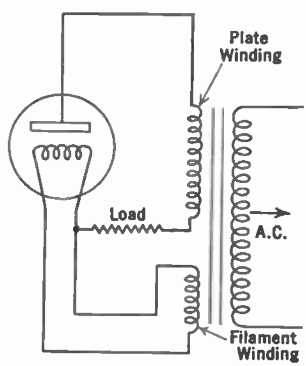


FIG. 249.—Tungar rectifier circuit.

A diagram of the connections of a typical tungar rectifier are shown in Fig. 249. It consists of a transformer to reduce the input a.-c. voltage from 115 to from 30 to 75 volts; the tube itself, which is a simple two-element tube, consisting of plate and filament. The type in general home use is a 2-ampere charger, which means that it will put into a three-cell storage battery a current of 2 amperes.

Such chargers have been made to charge high-voltage batteries, say up to 45 volts, but at a reduced rate of about one-half ampere. The use of a.-c. tubes, however, will reduce the number of receivers which use d.-c. tubes, batteries, and chargers.

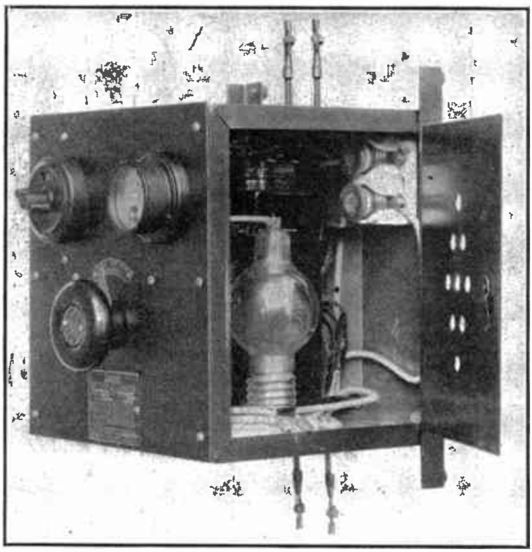


Fig. 250.—A typical Tungar rectifier.

The theory underlying the Tungar rectifier does not differ essentially from that already described for the filament and gaseous types of tubes. The filament supplies the electrons which bombard the inert gas and thereby produce more electrons and enable such a heavy current as 2, or even 5 amperes in the case of larger tubes, to be carried across the space between plate and filament. A tube similar to the Tungar is the UX–866, which will supply upwards of a half kilowatt without excessive voltage loss or heating. Others will supply 30 kw. or more.

325. The copper oxide rectifier.—The copper oxide rectifier is outstanding among rectifiers by virtue of its simplicity and reliability. The rectifier consists of a sheet of copper on one side of which has been formed a coat of cuprous oxide (Cu_2O). Properly made, this combination has relatively low resistance in the direction oxide-to-copper, with very high resistance in the reverse direction.

The units are generally made in the form of washers, of 1½ inch outside diameter. These washers are then assembled in any desired series and parallel arrangement on mounting bolts. Soft metal washers are placed between the oxide layer and the adjacent metal surface for the purpose of improving the contact with the oxide. The surface of the oxide is graphitized for the same reason.

This rectifier operates electronically and not electrolytically. Rectification commences instantly on the application of voltage, with no forming or transient condition interposed. Current is carried not at points but uniformly over the available area. Furthermore, the rectifying elements can be paralleled to any extent. Operation in series presents no difficulties, as the discs divide the voltage with approximate uniformity.

The outstanding feature of the rectifier is its long life. Units on continuous duty life test, with battery load, show a reduction of a little over 20 per cent in charging current in 3½ years' operation. This is remarkable performance for a rectifier, since it operates entirely without attention or maintenance.

There are no limitations to the application of the copper oxide rectifier. It may be used either half wave or full wave. The bridge connection is commonly used since it simplifies the transformer design and furthermore permits units to be operated direct from the a.-c. line without intervening transformer if so desired. The quality of the d.-c. wave obtained is excellent so that filtering is readily accomplished. Battery charging, battery elimination, magnet operation, loudspeaker excitation, etc., in fact almost any d.-c. application can be successfully handled by the copper oxide rectifier.

326. Filter circuits for tube rectifiers of the filament type.—There are several kinds of rectifier tubes as described in Section 319. The filament type is the simplest to understand and perhaps the most commonly used and for this reason has been described in detail.

The output of the rectifier circuit is not an even flow of current at all. In a loud speaker it would make considerable noise, or if used in a radio receiver without further alteration the hum would be intolerable. The next step after rectification is filtering.

A good plate voltage supply device, then, consists first of a transformer which raises the a.-c. voltage to the value required by the receiver plus the losses in voltage in rectifier, filter and voltage divider. Second, the rectifier which performs the task already described. In the third place comes the filter whose task it is to smooth out the pulsations of current in the plate circuit of the rectifier so that the final product will be d.c. of constant amplitude and a minimum amount of a.c. in it, and of a voltage high enough to supply the voltage and current required by the receiver and amplifier as well as the losses in the device itself.

A conventional filter circuit consists of series inductances which smooth out the ripples of current and keep the current flowing at the a.-c. voltage reversals, and shunt condensers which act as reservoirs of voltage as described in Section 73. A two-section filter is shown in Fig. 248, that is, two chokes and their accompanying condensers. The amount of filtering necessary depends entirely upon the amount of residual hum that is tolerable after the filtering has taken place. A very quiet power supply device is required in those receivers which have a rather high audio-frequency voltage amplification and which amplify frequencies as low as 120 to 60 cycles.

There is always a certain amount of a.-c. voltage left after the filtering has taken place. This voltage is a matter of millivolts compared to several hundred volts of d.c., but even these small a.-c. voltages may become objectionable when a loud speaker that is efficient at low frequencies is used. This voltage is a combination of the fundamental frequency, 60 cycles, and its harmonics. In double-wave power supply devices the second harmonic or 120 cycles is particularly strong.

A good loud speaker which reproduces notes as low as 120 cycles will hum badly when used with a power amplifier which gets its voltages from a poorly filtered supply. Even with a very good filter, some a.-c. voltages are likely to be picked up by the cores of audio transformers if they are near power transformers carrying a.-c. currents. The ultimate extent to which hum may be reduced may be the amount that transformers can be shielded from stray fields, and not the extent to which a rectifier's output may be filtered. The push-pull amplifier may be operated from incompletely filtered supply. The rest of the current required from the B eliminator can be carefully filtered at reduced cost.

327. Regulation.—After passing through the filter the circuit returns to the transformer through the terminal resistance which acts as a potentiometer to reduce the full voltage to the values desired. If the full voltage is 180 volts, a tap at the proper place will give 90 volts and another will give 45 volts for the detector tube. Now it is apparent that the voltage across this resistance depends upon the current through it, and if there were no other resistances in the circuit Ohm's law would tell us at once what the voltage across the resistance would be. Unfortunately the transformer, the rectifier tube, and the filter chokes all have resistance, so that the greater the current taken from the whole device the lower is the voltage across its output. From batteries one gets 90 volts for his tubes whether he runs one or a dozen of them; the drain from the batteries is all that changes. With a voltage supply device, however, the voltage at the amplifier tap would be less than 90 if the current taken from it exceeds a certain amount. This is a distinct disadvantage from every standpoint but one.

In a high-resistance system it is difficult to blow up tubes. If a B battery is put across a tube, the filament immediately becomes very bright and probably burns up because too much current goes through it. The current that can be taken from a high-resistance device is limited and so it is doubtful if enough current could be secured to damage the tube. This, however, is a rather dubious advantage.

A series of curves showing the output voltage at various output current drains gives what is known as the regulation of the device, that is, the manner in which its voltage drops with increase in current taken from it. The history of plate supply devices can be traced in a record of the regulation of such units, the older they are the worse their regulation curves, or the higher their internal resistance. The steep regulation curve of an early "B eliminator" may be seen in Fig. 251.

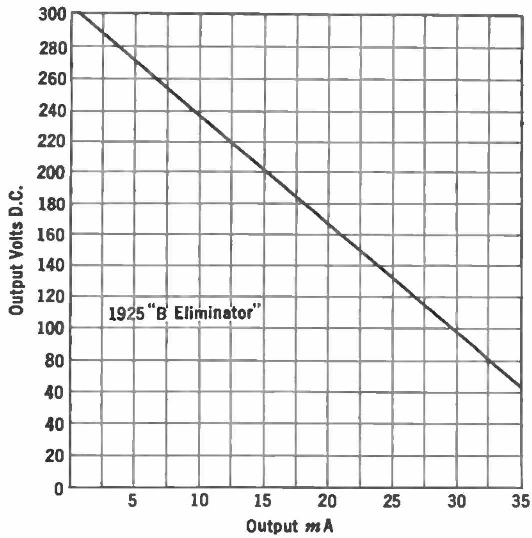


Fig. 251.—Regulation curve of early "B eliminator." Note the great voltage drop.

328. A typical rectifier-filter system.—Several curves showing the relation between the current and voltage in a modern rectifier-filter are shown in Fig. 252.

The losses in voltage are those due the IR drop in the resistance of the tube and the transformer. In Fig. 252 the voltage across the output resistance of the filter would be less than these voltages by the drop in the filter resistance. If the filter chokes have a d.-c. resistance of 1000 ohms there would be an additional drop of 1 volt per milliampere of current from it.

A transformer which supplies 220 volts to each plate of a CX-380 tube will deliver a voltage of 220 across the input to the filter and if the latter has a resistance of 1000 ohms about 150 volts will appear across the output at a current drain of 65 ma.

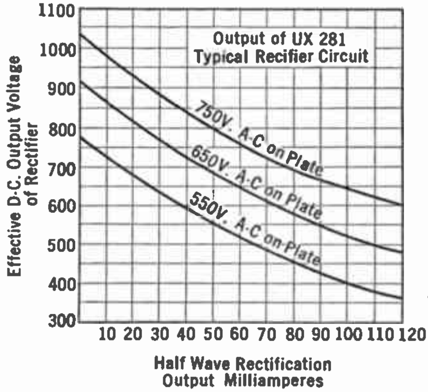


FIG. 252.—Output of modern rectifier.

The variations in transformer voltage, current through the tube, and steady load current are shown in the oscillographs in Fig. 253. The fact that abnormally high instantaneous values of currents must be passed by the tube is clearly shown in the tube current wave. No current flows until the transformer voltage reaches a certain minimum value and current ceases to flow as the voltage across the transformer secondary decreases. The peak current rises as high as 310 milliamperes; and on the assumption that the resistance of the tube remains constant, the power lost in it increases as the square of the current, showing that this high current puts a severe burden on the tube. As a matter of fact the internal resistance of the tube is almost constant, decreasing somewhat at higher current loads.

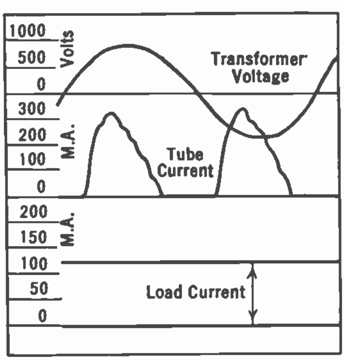


FIG. 253.—High instantaneous current required from rectifier with capacitive input.

If the first filter condenser is removed and placed across the output, as shown in Fig. 254, not only does the peak current passed by the tube decrease, thereby decreasing the power lost in it, but the regulation is improved. The disadvantage of such a connection is slightly greater hum output and the fact that the output voltage is decreased by about 20 per cent. This loss in voltage may be made up by increasing the secondary voltage of the transformer,

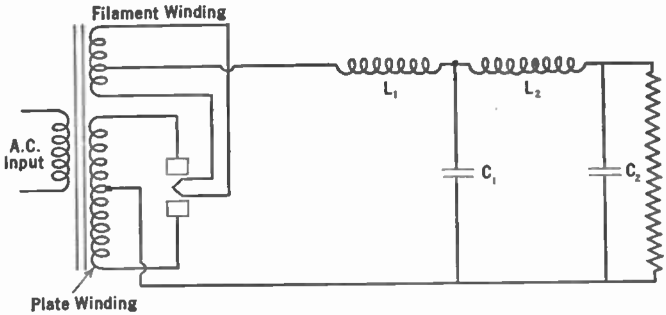


FIG. 254.—Inductance input type of filter.

and even then the power losses in the tube will be less. The peak current passed through the tube in the second case is about 140 milliamperes when a steady current of 125 ma. is required, thereby reducing the power losses in the tube by about 35 per cent. Figure 255 shows the oscillograph studies of such a filter-rectifier system.

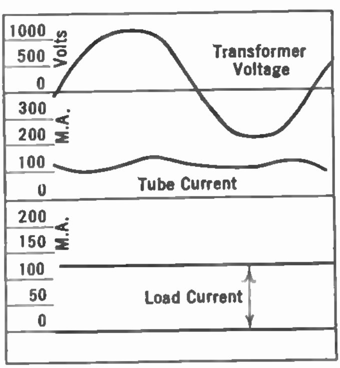


FIG. 255.—Reduced tube current in an inductance input filter.

The connection which omits the first filter condenser increases the life of the tube, permits the use of a tube whose emission has fallen below the point at which the tube would be useless in a capacity input filter, gives better regulation at current drains over 20 ma., reduces the filament emission required, and reduces the heating of the tube.

329. Hum output.—Using chokes of 11.5 and 13.5 henrys respectively for L_1 and L_2 and a 4-mfd. and an 8-mfd. condenser as C_1 and C_2, a hum output of 44 millivolts is reported as a typical case. Whether or not this amount of hum is objectionable depends upon a multitude of factors including a matter of personal opinion. The amount of hum that some listeners can tolerate would take away all the enjoyment of radio from other listeners. Improvement in loud speakers and amplifiers will make necessary greater refinements in the way of eliminating hum, whether due to imperfect filtering, the use of a.-c. tubes or pickup from nearby wiring, or iron cores carrying a.-c. currents.

Although the amount of hum that can be tolerated is a matter of opinion, the following figures may be interesting. Using a sensitive moving-coil loud speaker in a 3-foot baffle, a 120-cycle voltage of 0.54 across the primary of the transformer feeding the loud speaker was too loud for comfort. A voltage of 0.15 volt was a desirable maximum. At 60 cycles these voltages were 5.2 and 1.3 respectively.

Hum measurements on twelve popular socket power devices sold during 1927 gave the following r.m.s. voltages expressed as percentages of the d.-c. output voltage. (To get the effective a.-c. millivolts multiply by 10 times the d.-c. voltage.)

Load Current	Minimum	Maximum	Average
20 ma. from power tap	0.007	0.67	0.025
40 ma. from power tap	0.009	1.0	0.05
1 ma. from detector*	0.001	0.15	0.015
5 ma. from detector*	0.002	0.26	0.03

* 25 ma. load from power tap.

330. The voltage divider.—After the output of a rectifier has been properly filtered it is necessary to feed it to the tubes which need it. The power tube, or tubes, will require the greatest voltage and the other tubes in the set will probably require 90 and 45 volts. A voltage divider is necessary as a distributing system taking care that each set of tubes gets its required voltage. It consists of merely a resistor, or resistors, with taps at appropriate points so that the full voltage is across the power tube and lower voltages at other points in the system.

For example a rectifier-filter system may provide a total output of 220 volts under load. This is the voltage measured between the most positive and the most negative points in the circuit. Part of this voltage, 40 volts for example, can be used to supply *C* bias to the power tube. This leaves 180 volts which may be applied between the filament and the plate.

Let us consider the preliminary diagram in Fig. 256. Disregarding for the moment the resistance across the B voltage terminals, it may be seen that the plate of the tube gets its positive potential by being connected to the positive end of the plate supply unit. The negative end of the unit is connected to the center of the filament through a resistance. The plate current must flow through this resistance and there is a voltage drop across it. The grounded end of the B plate supply unit is the most negative point in the circuit. Going through the resistance toward the filament and thence toward the plate through the tube we proceed steadily toward a more positive point in the circuit. The filament end of the *C* bias resistor marked (+) is at a higher or more positive potential than is the grid end. The grid end, then, is negative and the voltage drop across this resistor, due the plate current flowing through it, may be used as the *C* bias for the tube. The voltage actually between the center of the filament and the plate is the total voltage across the plate supply unit minus the *C* bias voltage; or in case a 171 is the tube, the plate supply unit must have a terminal voltage of 220 in order to place a voltage of 40 between grid and filament and a voltage of 180 between plate and filament.

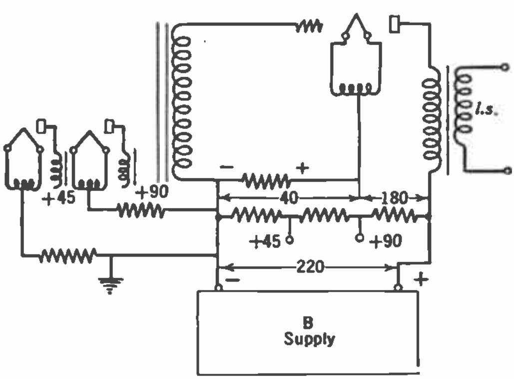


Fig. 256.—How the voltage divider originates.

It is now only necessary to place a resistance across the plate voltage supply unit so that various voltages appear along it, each voltage being less than the voltage across the two ends. It is only necessary to fix the values of the taps so that the voltages desired are attained.

If another *C* bias is needed another resistor can be connected to the negative end of the plate voltage supply and the filament of the tube requiring the bias. The plate current of that tube flowing through the new resistor to return to the filament, the source of the electrons, will cause a voltage drop across the resistance the negative end of which is toward the grid of the tube in question.

There is another method whereby the 40-volt bias for the power tube is tapped and lower voltages are obtained for other tubes. Such a method is liable to lead to unwanted couplings between tubes. For example, in a radio-frequency amplifier such a method of obtaining bias may lead to regeneration or even oscillation because the plate current of some tubes flows through the *C* bias of other tubes.

Both these *C* bias connections are shown in Fig. 257. One set is in series, the other is a parallel set. The importance of by-passing all such resistors has been mentioned in Section 233. A better method is to make the voltage divider part of the amplifier, as in Section 233. It is only necessary then to supply one B plus voltage to the amplifier.

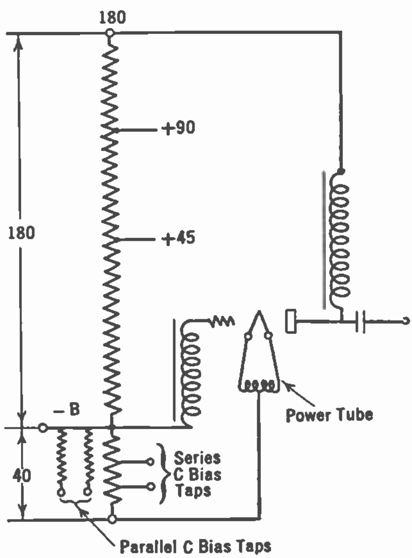


FIG. 257.—Both series and shunt *C* bias resistances are illustrated.

331. C bias for tubes operated from a.c.—When a tube is operated from a.c. the voltage across the *C* bias resistor must be slightly different than when the tube is operated from d.c. For example let us consider the operation of a 171 tube from a storage battery and from an a.-c. filament transformer. When the battery is used the 40.5-volt C battery is connected to the negative filament terminal, which is considered as the basis of reference to which all other voltages are measured.

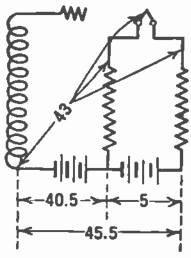


FIG. 258.—*C* bias in battery operated tube.

When the battery is replaced by an a.-c. transformer, the basis of reference for both B and C voltages is no longer one side of the filament because this is rapidly changing its polarity with the changes in polarity of the a.-c. voltage. The new basis is the exact electrical center of the filament, which is not far from the mechanical center. The B and C voltages are connected, not to one side of the filament but to the fictitious center of the filament by means of a center tap on the lighting transformer or to a center tap on a resistor. Let us suppose a transformer is used with negligible resistance in it.

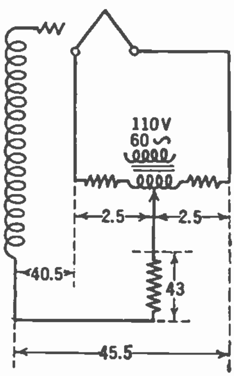


FIG. 259.—*C* bias introduced by plate current flowing through resistance.

In Fig. 258 is the d.-c. case in which the filament resistance is represented as divided in half and placed in each leg. The *C* voltage is connected to the negative leg, and the voltage measured from negative and plus *A* are shown. Between the center of the electron source and the point where the *C* bias enters the system is half the filament resistance across which is half the total voltage drop or 2.5 volts, and so the *C* bias with respect to the true center of the filament is 43 volts. When the *C* bias is introduced by means of a resistor into the center tap of a transformer (Fig. 259) the voltage drop across this resistor—to take care of the 2.5-volt drop across half of the filament—must be 43 volts. Then at the two ends of the filament are voltages of 43 − 2.5 or 40.5 and 43 + 2.5 or 45.5, giving as an average 43 volts as before.

Now suppose we put a resistance across the filament with the center tap on it, as in Fig. 260. What must be the voltage drop across the *C* bias resistor to provide 43 volts to the center of the filament? If this voltage is 43 volts, the voltage at the two ends of the filament will be 43 volts plus and minus the voltage drop in the resistance across the filament. This voltage drop is the plate current through the ohmic resistance of the center tapped device. Thus if the resistance is 100 ohms, and the plate current is 20 milliamperes, the voltage across each half of this filament will be 45 and 43, giving an average of 44 volts. Thus it is seen that each new condition demands some adjustment to get the required bias.

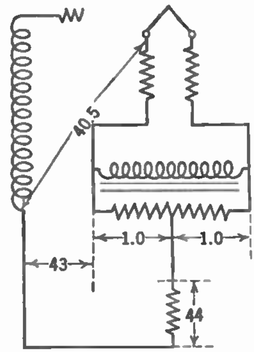


FIG. 260.—Grid resistance introduced into center of filament by mid-tap resistance.

332. Engineering the voltage divider.—The lower the resistance of the voltage divider, the better will be the regulation of the entire device, but the greater the load the tube must bear. In general a voltage divider is engineered as follows. In Fig. 261, suppose the current flowing through the resistance R_1 is 20 milliamperes. This is known as the " bleed " or " waste " current. It flows whether or not there are any tubes in the receiver that is supplied with voltage from the device. At the point *B*, a voltage of 45 is desired. The value of resistance is, according to Ohm's law, $E \div I$ and so is $45 \div 0.02$ or 2250 ohms. Since

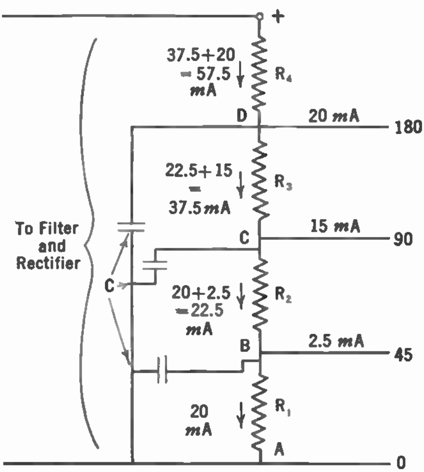


FIG. 261.—Designing the voltage divider.

this tap supplied only the detector plate circuit the current will be about 2.5 ma., and is added to the 20 ma. taken by the lowest resistance. Thus through R_2 flows 22.5 ma. and since 90 volts is desired at point C the resistance R_2 will be 45 ÷ 22.5 or 2000 ohms. If the tubes which require 90 volts take a total of 15 ma. from the plate voltage device, the final resistance will be 180 − 90 ÷ 37.5 or 90 ÷ 37.5 or 2400 ohms. The entire resistance will be 6650 ohms, with taps at 2400, 2000, and 2250 ohms. The greatest amount of power must be dissipated by the 2400-ohm resistor and so if the entire resistance up to R_4 is wound with wire large enough and on a frame that can dissipate the heat corresponding to 4 watts, there will be no trouble. Voltage dividers are available which consist of a single winding of resistance wire on a heat-resisting form. There are several sliders so that the correct voltages can be obtained easily.

If any a.-c. current remains and flows through the voltage divider an a.-c. voltage will be applied to the receiver to which this part of the voltage divider connects. Hum results. If, however, a condenser is connected from the high voltage end of this resistor to the negative terminal of the divider, and if its reactance to the a.-c. voltage is small the a.-c. currents will set up a small voltage across the low impedance of the resistor shunted by a high capacity.

Problem 1–16. The maximum voltage needed with the voltage divider of Fig. 261 is 180 volts, but the output of the filter is 200 volts under load. What is the value of resistance R_4 to reduce this voltage to 180 and what must be its power dissipation in watts?

Problem 2–16. Using a tube with a filament voltage of 7.5 volts and operated from d.c. the proper C bias is 50 volts. The plate current then is 25 ma. What is the voltage that must appear across the C bias resistor when the tube is operated from a.c. and when this resistor is connected to a center of a resistanceless transformer winding? What must be the voltage if the resistor connects to the center of a 100-ohm resistance?

Problem 3–16. What power in watts is dissipated in each of the resistances in Fig. 261 under the conditions of Problem 1–16?

Problem 4–16. The resistance of the filter is 300 ohms. What must be the output of the rectifier if the output of the filter is 250 volts and if 40 ma. flow through the voltage divider resistance R_4.

333. Voltage regulation.—In districts where the line voltages vary considerably from hour to hour or from day to day, trouble is had with the poor regulation. When the line voltage is high, the voltage is high, the voltages on the tubes will be high and their life will be short. When the line voltage goes down the voltages on the tube go down and the receivers do not work properly. Several methods have been worked out to alleviate this difficulty.

One method involves the use of a line voltage regulator or ballast lamp which passes 1.7 amperes (UX–876, C–376) at any voltage between 40 and 60. The lamp is connected in series with the primary of the power transformer. If the line voltage averages 115 volts, the load is so adjusted that 65 volts appear across the primary of the transformer and 50 volts across the tube. Then when the line voltage varies the voltage drop across the tube varies and the voltage across the primary remains at 65 volts. The chief difficulty with this tube is its slow action. It requires several minutes for a steady state to be reached.

A tube that has been used much more than the ballast lamp is the voltage regulator or "glow tube," the UX–874 or CX–374. This tube is placed across the 90-volt tap in the voltage divider. It is gas-filled and has a characteristic such that the voltage across it is constant at 90 volts at all currents from 10 to 50 ma. The tube has only two elements and the other two prongs of the base are shorted within the base. If one side of the a.-c. line is connected to the socket into which this tube fits, the line will be open unless this tube is in its socket and it thereby provides a certain factor of safety. Both tubes are shown in the circuit of Fig. 262.

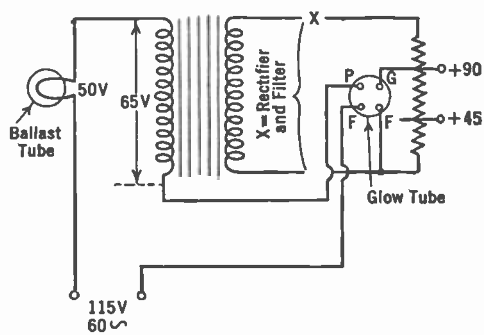


Fig. 262.—Ballast tube to maintain constant a.-c. voltage input to power transformer.

The use of a simple series resistor between the line and one side of the primary of the power transformer has been advocated and practiced a great deal. It has only one virtue, the voltage on the receiver can never get higher than a certain value which can be made below the point at which tube life is threatened. If the voltage goes down, however, nothing can bring back the voltage across the receiver to its correct value unless the series resistance is shorted.

The problem will probably resolve itself into one of making tubes which can stand the voltage variations that are to be encountered in practice, or in developing foolproof systems for maintaining constant the voltage input to the receiver.

CHAPTER XVII

OSCILLATORS, TRANSMITTERS, ETC.

BECAUSE a tube acts as an amplifier, it can be made to generate a.-c. currents of constant amplitude and at frequencies covering the entire range from one or two cycles per second to well over 300 million cycles (one meter). Because the energy in the plate circuit of the tube is greater than exists in the input or grid circuit, some of this energy can be fed back by several ways into the input circuit and there amplified again. Starting with an initial oscillation in the grid or plate circuit, provided the coupling between input and output circuits is of the proper phase and magnitude, this oscillation can be repeated and amplified, until finally the tube maintains stable oscillations without the necessity of exciting the grid from any outside circuit.

Before endeavoring to learn how a tube oscillates, etc., we should get an idea of what the term " oscillation " means.

334. Oscillating circuits.—One of the most famous experiments in all radio history is that of charging a condenser and letting it discharge through a resistance and an inductance. If the resistance takes the form of a gap (Fig. 263) in the circuit across which a spark jumps, a photograph of this spark made on a rotating mirror oscillograph shows that during the instant of discharge the spark jumps back and forth across the gap several times, first in one direction and then in another.

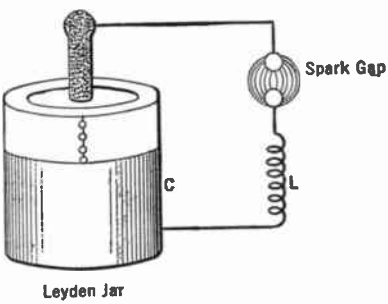


FIG. 263.—Familiar Leyden jar.

In other words the current in the condenser surges back and forth across the gap instead of making one spark and thereby thoroughly discharging the condenser.

Now such a circuit will produce an oscillatory spark in the manner just explained if the resistance, inductance, and capacity have correct values. When such an oscillatory spark takes place, electric waves are set up in the ether. These waves have a frequency determined by the well-known expression:

$$f = \frac{1}{2\pi\sqrt{LC}}.$$

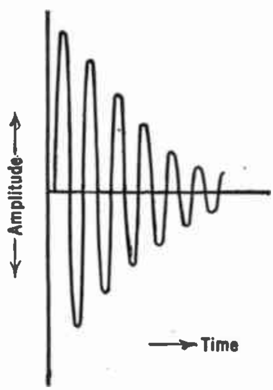


FIG. 264.—Highly damped series of waves.

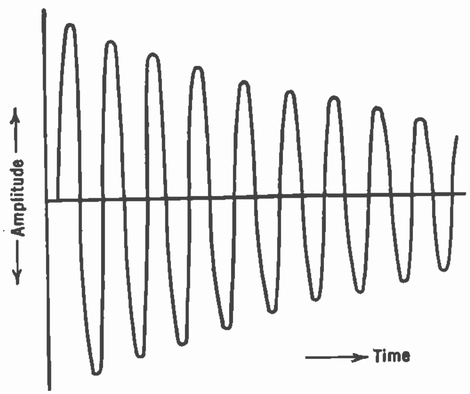


FIG. 265.—Slightly damped (low resistance circuit) waves.

If the resistance is too great, the spark will not set up such waves. The circuit is then non-oscillatory. If the resistance is decreased to a very low value, the number of oscillations that take place before the spark finally dies out becomes very great.

Thus in Fig. 264 the circuit has a high resistance; only a few oscillations take place and these at a rapid reduction in amplitude, each from the other. In Fig. 265 the resistance is very low and many oscillations take place, the amplitude falling off slowly. A circuit with much resistance is called **highly damped** because the waves decrease in amplitude—are damped out by the resistance—at a rapid rate. An **undamped** or continuous wave is generated by a theoretical circuit with no resistance, or one in which there is a device which supplies the power wasted in the various resistance.

335. Undamped or continuous oscillations.—With a given circuit, if the resistance can be reduced to zero through some means—adding a negative resistance, for example, the damping factor due the resistance is wiped out and the circuit generates continuous-amplitude or undamped waves.

336. The amplifier as an oscillator.—Consider the box in Fig. 266, which is an amplifier. Any voltage put into it reappears in the output magnified by the amplification factor of the device. Suppose that the input is composed of a coil and condenser, and that part of the output voltage can be coupled to the input coil. At the start suppose this coupling coil *T*, commonly called a tickler, is short-circuited, or removed from the input coil. Now if the condenser *C* is charged and then allowed to discharge suddenly by closing the key, *K*, oscillations will be set up which will die out at a rate depending upon the resistance of the coil and condenser.

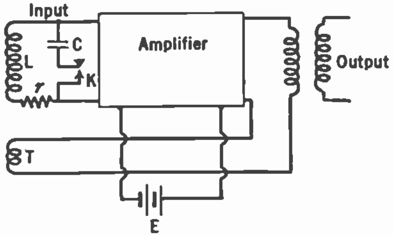


FIG. 266.—Essentials of an oscillator—an amplifier and feedback from output to input.

In the output circuit of the device will reappear an amplified version of these oscillations. They too will die out. The energy in them comes from some local battery, *E*, and the oscillations in the input circuit only serve to release some of this local energy. Now couple the tickler coil to the input in such a manner that the voltage induced into the input coil by ordinary transformer action is in phase with the oscillatory voltage. Then when the switch is closed, a voltage appears across the input, is amplified in the device, and in amplified form is impressed back on the input. This will cause an increase in the oscillatory voltage, and so the effect will be an ever-increasing series of oscillations, as in Fig. 267.

Ordinary oscillations are started in a tube circuit by thumping the tube, or by turning on the plate battery, or by any sudden change in the electrical or mechanical constants of the circuit.

Oscillations in some circuits require appreciable time to build up to their final value. For example a loud speaker which "feeds back" mechanically into the elements of a detector tube may finally result in a steady howl. If the loud speaker is near the detector tube, or standing on the receiver cabinet, this chain of events may occur. A sudden jar causes the elements in the detector to change their relative position. This change takes place at an audio rate depending upon the natural mechanical frequency of the element in question. This audio tone is amplified by the following tubes and finally comes from the loud speaker. The air waves from the loud speaker strike the tube and set the elements into even greater vibrations and finally the whole system howls, or oscillates at an audio rate. Microphonic tubes, particularly those with very small filaments, are prone to "bongs" which may be amplified and lead to steady howls which take a second or two to build up to final intensity.

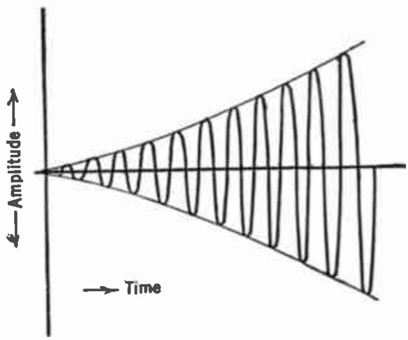


FIG. 267.—Building up of oscillations in resistanceless circuit or amplifier circuit.

337. Conditions for oscillation.—Oscillations depend upon the coupling between output and input, upon the fact that the device, usually a tube, can amplify, and the fact that a combination of inductance and capacity exists with resistance of such values that the oscillations have the desired frequency. It is more difficult to start and to maintain oscillations in a high-resistance circuit.

If the mutual inductance between grid coil and tickler is sufficient to start oscillations, it can be loosened with an increase in current. If the power in the oscillatory circuit is measured, it will be found to go through a maximum when the effective resistance

$\left(\frac{L^2\omega^2}{r}\right)$ becomes equal to the tube plate resistance. If the C bias on the tube is varied, it will be found that another value of mutual inductance will be necessary to make the tube oscillate. All these factors must be adjusted properly if maximum oscillatory power is to be supplied by the tube.

338. Maximum oscillatory plate current.—The oscillating tube may be thought of as an amplifier in which the exciting or input voltage which is amplified comes from the tube itself; in other words it is a self-excited amplifier. An alternating current flows in its plate circuit just as in any ordinary amplifier. What is the maximum value of this current?

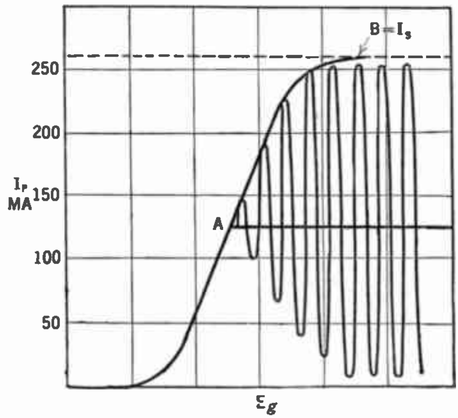


FIG. 268.—Manner in which oscillations beginning in tube circuit build up until entire characteristic of tube is utilized.

Consider the tube working at the point A in Fig. 268. When oscillations start, the a.-c. plate current increases from a small value during the first few oscillations until it goes from zero to double the d.-c. value at A if a sine wave is being generated, or until the plate current curve flattens out. Then an increase in excitation does not result in an increased plate current (a.c.). The limit has been reached for the a.-c. plate current.

If the current at B is the saturation current, I_s, of the tube, the maximum a.-c. plate current will be

$$I_p = \frac{I_s}{2}, \qquad (1)$$

and because the a.-c. plate current is equal to the a.-c. grid voltage multipled by the mutual conductance of the circuit, or $I_p = G_m E_g$,

$$E_g = \frac{I_s}{2\,G_m}, \tag{2}$$

which is also equal to the voltage induced in the grid coil by an a.-c. current flowing through the plate coil. This voltage is the current in the oscillatory circuit multiplied by the mutual reactance, or

$$E_g = I_L M\omega \tag{3}$$

from which we can calculate the current through this coil,

$$I_L = \frac{E_g}{M\omega} = \frac{I_s}{2\,G_m M\omega} \tag{4}$$

$$= \frac{I_s}{2\sqrt{2}\,G_m M\omega}\ \text{(r.m.s.)} \tag{4a}$$

Example 1–17. Suppose the saturation current of a power tube is 100 milliamperes (a low figure) and the other constants in Fig. 271 are L = 500 μh, r = 10 ohms, R_p = 7150 ohms, $G_m = .76 \times 10^{-3}$, M = 160 μh, f = 100 kc. What is the peak and r.m.s. oscillatory current, that is, the current through the inductance, L, and what is the grid voltage due this current?

Solution.

$$I_L = \frac{I_s}{2\,G_m M\omega}$$

$$= \frac{100 \times 10^{-3}}{2 \times 6.28 \times 100{,}000 \times .76 \times 10^{-3} \times 160 \times 10^{-6}}$$

$$= 0.655 \text{ ampere} = .465 \text{ r.m.s.}$$

$$E_g = I_L M\omega$$

$$= .655 \times 160 \times 10^{-6} \times 6.28 \times 10^5$$

$$= 66 \text{ volts.}$$

Problem 1–17. The voltage across the condenser in the tuned circuit of the above example is equal to the current through it (which differs but little from I_L) times the reactance of the condenser at the resonant frequency. Calculate the voltage across the condenser. The power used up in heating the resistance of the coil is $(I_L)^2 \times r$. Calculate this power (use the r.m.s. value of I_L). Let this be called the useful power supplied by the tube. The power from the plate battery is the product of the plate voltage and the plate current = $I_p \times E_p$. If the steady plate current is 50 milliamperes and the efficiency of the system is 50 per cent, calculate the plate voltage necessary. The efficiency is the ratio of the power supplied to the tuned circuit to the total power supplied to the tube. Calculate this voltage.

Thus,
$$E_c = I_c \times X_c$$
$$P_r = I_L^2 r$$
$$P_T = E_p \times I_p$$
$$\text{eff.} = \frac{P_r}{P_T}.$$

339. Effect of coupling.—If such a circuit is set up in the laboratory, it will be found that oscillations occur over a rather wide range of coupling. Any one who has operated a regenerative receiver for short, medium, or long waves knows that the loudest signals are received just before the tube stops oscillating due to too loose coupling between the secondary or grid coil and the tickler.

Looking at formula (3) we see that the induced grid voltage, due to the oscillatory current, is proportional to the coupling between the grid and plate coils. This induced voltage must be at least equal to the original voltage there due to the condenser discharge in order that the oscillations may be built up. If the induced voltage is less than the original voltage, oscillations will last longer than if the tube were not present, but they will finally die out. The effect is as though we had reduced the resistance in this oscillatory circuit but had not completely removed it. When the induced voltage is equal to the original voltage, we have in effect reduced to zero the resistance of the circuit, and oscillations can keep up, although feebly. If, now, the induced voltage is increased all of the losses in the input circuit will be made up by the power taken from the local batteries (the plate battery) and continuous oscillations will take place, gradually increasing in amplitude until the entire characteristic of the tube is used.

If we start oscillations, and then decrease the coupling, and if E_g (induced) is to remain the same, the oscillatory current must *increase*. Thus, when the coupling is loosened, but not enough to stop oscillations completely, the oscillatory current actually increases to make up the loss in induced voltage due to the decreased coupling. When the whole plate current characteristic is used by these oscillations, further decrease in coupling must decrease the exciting grid voltage, E_g, and oscillations cease.

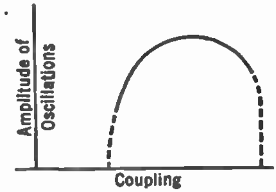


FIG. 269.—Effect of coupling between in- and output circuits.

If, on the other hand, the mutual inductance is increased, oscillations rise to a maximum and then fall off and finally cease entirely. The reason in this case for cessation of oscillations is different from the above reason. It is due to an increase in the effective resistance of the tuned circuit, so that greater exciting voltage is necessary to overcome the increased losses.

The manner in which coupling affects amplitude of oscillatory current may be seen in Fig. 269.

340. Dynamic characteristics.—Because a change in grid voltage produces a change in plate voltage—just as in a resistance-coupled amplifier (Section 176), we can not use the static characteristic curves to predict the action in the tube. We must use the dynamic curves. In Fig. 270 are the static characteristic curves of a low-μ oscillator tube. When the grid voltage increases in a positive direction due to the exciting or induced voltage, E_g, the plate current increases but the voltage actually on the plate decreases because of the greater IR drop in voltage across the

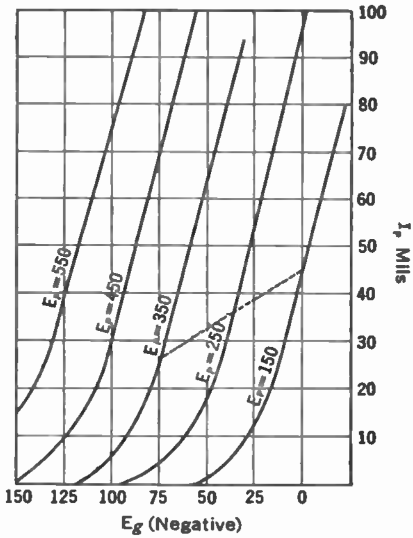


FIG. 270.—Characteristic curves of power oscillator tube. The dotted line is the dynamic curve used when the tube oscillates.

plate load. The operating point then may move along a curve like the dotted line. Because of the decreased slope of the dynamic curve compared to the static characteristic, the mutual conductance has decreased too, and it is not strictly correct to use the static value in equations (1), etc. It is approximately correct, however, unless the load in the plate circuit has a very high effective resistance, for example, a low-resistance circuit. In practice this load is made up of not only the resistance always in the circuit but the resistance "reflected" into it by transformer action by coupling an antenna to the plate coil by means of a mutual inductance and so has a fairly low effective resistance.

Modern tubes have such high values of saturation current that they are never operated at the point at which the d.-c. plate current is half the saturation value. Instead, they are so biased that the average value is such that the power dissipated on the plate is within the limits of safe heating. Then if sine waves are generated, the maximum value of the a.-c. plate current is twice the value read on the d.-c. meter. This value should be used in problems and examples instead of the saturation value. For example a UX–210 has a saturation current of an ampere or more, but such a tube could never be operated so that the d.-c. plate current would be of the order of 500 ma. Instead it is usually less than 100 ma.

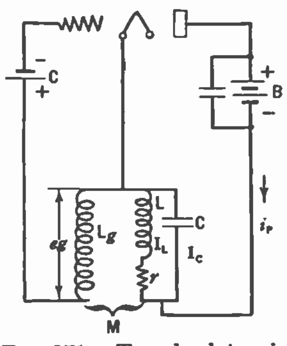


FIG. 271.—Tuned plate circuit (grid tickler) oscillator.

341. Conditions for oscillation.—When the tube and circuit oscillate we can state that the resistance of the LCR circuit has been decreased to the point that any oscillation starting there will not be damped out. In other words, if the resistance of the circuit is R, we must supply $-R$ to it in order to get sustained oscillations.

In the circuit shown in Fig. 271 the value of resistance of the circuit when coupled to the grid coil is

$$R + \frac{L \pm \mu M}{CR_p}.$$

Now all of the factors in this equation are positive with the exception of M which may be either positive or negative depending upon how L is coupled to the grid coil. When it is connected so that oscillations occur, M is negative, and so the resistance R, in the oscillatory circuit is decreased. If the coupling coil is reversed, the total resistance in the oscillatory circuit is increased, and of course sustained oscillations cannot be built up. By making L, C, and M have the proper value, we can either add resistance to the oscillatory circuit—and then no oscillations are possible, decrease the total resistance to zero, or make it negative. The latter case is true when $\frac{L \pm \mu M}{CR_p}$ is greater than R.

The conditions for oscillation then are:

$$\frac{L + \mu M}{CR_p} \geqq R. \quad . \quad . \quad . \quad . \quad .$$

or

$$M \geqq C \frac{R_p}{R}\left(R + \frac{L}{CR_p}\right) = \frac{L}{\mu} + \frac{CRR_p}{\mu}$$

or

$$\frac{\mu}{R_p} M \geqq CR + \frac{L}{R_p}$$

or

$$G_m M \geqq CR + \frac{L}{R_p}$$

where the sign $\geqq$ means " is equal to or greater than,"

and $\pm$ means " plus or minus."

A number of facts can be gathered from these formulas. The better the tube, that is, the greater its mutual conductance, G_m, the looser can be the coupling and still maintain oscillations; with a given tube whose mutual conductance is fixed, and with a given coil-condenser combination, a certain mutual inductance is required to start and maintain oscillations; the greater the resistance in the tuned circuit the better the tube must be with a given mutual to maintain oscillations.

Problem 2–17. The mutual conductance of a power tube is 1500 micromhos, its amplification factor is 7.6 and its plate resistance is 3500 ohms. It is desired to generate oscillations of a frequency of 1000 kc. The coil to be used, in a tuned plate circuit as in Fig. 271, has an inductance of 200 microhenrys and a resistance of 10 ohms. Calculate the mutual inductance required to maintain oscillations. If the peak plate current is 100 ma.:—

What is the maximum current, I_L, that can exist in the oscillatory circuit? If the power in this oscillatory circuit is $I_L^2 \times r$ and r is its resistance (10 ohms) what is the power dissipated there?

342. Efficiency of an oscillator.—As in an amplifier, when the grid is not excited, the power taken from the plate battery is equal to I_pE_p, and this power is dissipated in heating the plate of the tube. When oscillations take place the plate current and plate voltage vary about their average or non-oscillating values. The power taken from the battery does not change, but the power wasted in heating the plate decreases, part of it going into the load —just as in an amplifier (Section 189).

If the operating point is such that when the tube oscillates its maximum a.-c. is twice the value read in a d.-c. meter and once in each cycle is just reduced to zero plate current, the efficiency is 50 per cent. In Fig. 268 the average plate current is 0.125 ampere. The minimum value it can reach is zero and the greatest value it can reach is twice this value of 0.25 ampere. At the same time the plate voltage variations are from zero to twice the average value. In other words the variations in plate current are 0.125 ampere plus and minus 0.125 ampere, and the plate voltage is E_p volts plus and minus E_p volts. This is an a.-c. voltage whose maximum value is E_p volts, and an a.-c. plate current whose maximum is 0.125 ampere.

The power, as in a resistive a.-c. circuit, is the product of the effective current and the effective voltage, or

$$P = \frac{E_p}{\sqrt{2}} \times \frac{I_p}{\sqrt{2}} = \frac{E_pI_p}{2},$$

and since the power supplied by the plate battery is E_pI_p, one-half the power taken from the battery is wasted in the tube and one-half is used in overcoming the resistance losses in the oscillatory circuit.

If we rate the efficiency of the plate circuit as the ratio between the total amount of power taken from the B battery, I_pE_p, to the power used in the oscillatory circuit, $\frac{E_pI_p}{2}$, we see that the above condition represents an efficiency of 50 per cent.

If the C bias of the tube is so adjusted that the operating point goes down on the lower bend, the steady plate current is small, and the power taken from the battery is small. As shown in Fig. 272, plate current flows only when the grid gets sufficiently positive to permit it, that is, when the operating point gets up far enough on the plate current curve for current to flow. Thus current flows during only a part of the cycle, and because the a.-c. components decrease less rapidly than the average value of current, the efficiency may increase above 50 per cent.

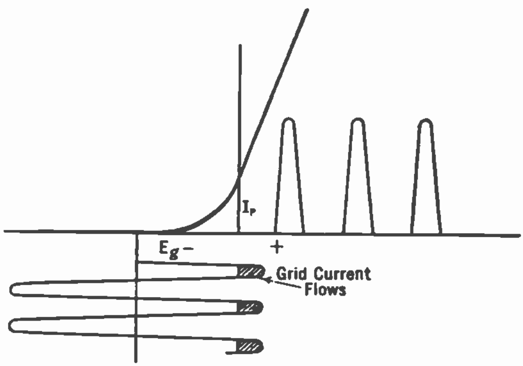


FIG. 272.—Form of plate current waves when tube is so biased that lower part of characteristic is used.

343. Harmonics.—If a large C bias is used, the form of the oscillatory current is no longer a sine wave and of course many harmonics are generated. Thus an oscillator generating a wave form like that in Fig. 272 may be thought of as an oscillator producing a pure sine wave plus many harmonics. If the oscillator is used to supply power to an antenna which is tuned to the fundamental frequency, these harmonics put little power into this antenna provided it is coupled loosely enough to the tuned circuit.

On short waves this is of great importance, because of the carrying power of high frequencies. Thus if a tube oscillates at 40 meters and puts out even a comparatively weak second harmonic on 20 meters, the latter signal can be heard over an area of many hundreds or even thousands of miles. A broadcasting station operating on 500 meters with a strong second harmonic can ruin another station's program operating on 250 meters, and so on.

There are times when it is desirable to generate a wave form that has many harmonics, or a particular harmonic of large amplitude. For example a quartz crystal is frequently used to control the frequency of a transmitter. Because the thickness of the quartz plate varies inversely as the frequency, for a high-frequency circuit the crystal is very thin and there is danger of its breaking. For this reason a thicker crystal is used and a harmonic of the oscillator which it controls is used to drive a power amplifier which works into the antenna. The crystal circuit, then, is an oscillator which should generate a large second harmonic. By suitably adjusting the *C* bias such an output can be attained.

Such a highly biased tube will have strong harmonics of much higher order than the second, and if the frequency of the crystal is accurately known these higher harmonic components of the output of the tube can be used as standards of frequency over a very wide range. It is frequently possible to count up to the 50th harmonic of such a circuit. Thus if the fundamental frequency of the crystal is 500 kc., the 10th harmonic would be 5000 kc., and the 50th would be 25,000 kc.

344. Power output of an oscillator tube.—The power output from an oscillating tube depends upon the efficiency of the circuit and the amount of power that can safely be dissipated at the plate. If the circuit is 50 per cent efficient and if the tube can safely dissipate 50 watts on the plate, the output power is evidently 50 watts. If, however, a high *C* bias is used and a larger plate voltage, the steady power taken from the battery may increase appreciably but a smaller proportion of it is lost in the tube and of course more power into the load (the tuned circuit) obtained. Thus if the tube is 70 per cent efficient, and can dissipate 50 watts internally, the ouput power can be 116 watts and the total power supplied by the battery 167 watts.

When an amateur manages to put into his transmitting tube twice the power for which it is rated, he may still be operating the tube as required by the manufacturer. He has increased the efficiency of his circuit by operating at a high C bias, and by making his output far from sine wave in form. The power lost on the plate may still be within the manufacturer's limit, and the power obtained from the plate voltage supply unit and usefully employed in putting signals into an antenna may be considerably increased. If, however, his tube stops oscillating suddenly, due to some maladjustment, the full plate battery power must be dissipated at the plate and it is almost certain to be melted and the tube destroyed.

Problem 3–17. An amateur desires to get 100 useful watts from a so-called 50-watt tube. This means that 50 watts can be safely dissipated at the plate. How efficient must his circuit be? If the plate voltage is 1000 volts, what will be the plate current? If his antenna has a resistance of 60 ohms at 40 meters, what antenna current must be put into it to radiate 100 watts?

Problem 4–17. The grid voltage necessary to excite a given transmitting tube is 100 volts. The frequency is 500 kc., the tuned circuit inductance, L_2, is 200 microhenrys, the coefficient of coupling between grid coil and tuned circuit inductance is 0.3, the current in the tuned circuit is one ampere. What must be the inductance L_g of the grid coil?

$$E_g = M\omega I_L = M\omega \times 1.0$$
$$M = \tau\sqrt{L_g L_2} = .3\sqrt{L_g L_2}$$
$$\omega = 2\pi \times 500{,}000.$$

Problem 5–17. The resistance of the tuned circuit when coupled to an antenna is 30 ohms. Its inductance is 300 μh, the μ of the tube is 8, its plate resistance is 5000 ohms, the frequency is 300 kc. What must be the value of M to make the circuit oscillate? $\left[M = \frac{CR_p}{R}\left(R + \frac{L}{CR_p}\right)\right]$.

Problem 6–17. The normal plate current of a UV 203–A tube is 125 milliamperes at a plate voltage of 1000. If the circuit is 65 per cent efficient, how much can the plate current be increased at this voltage without using more than 50 watts on the plate? What is the input and the output power under these conditions?

It is possible to get circuits of high efficiency by increasing the C bias so that plate current flows only during a part of the cycle when the grid is positive. At these times the plate current is high, but at the same time the voltage actually on the plate is low—because of the fact that the grid and plate voltages are 180° out of phase and because of the high voltage lost in the load when the current is high—and so the power wasted at the plate is low. If the voltage at the plate could be reduced to zero no power would be lost there and the efficiency would be 100 per cent. Such conditions cannot happen, of course.

If the plate voltage is reduced to a value comparable to the grid voltage, the electrons from the filament would divide and more would go to the grid than ordinarily, with the result that the plate current would decrease. This would tend to increase the plate voltage, and so the limiting condition of zero plate voltage cannot be secured.

345. Maximum power output of oscillator.—As in an amplifier, the maximum power is converted from the battery to the load when the load resistance is equal to the tube plate resistance. Thus in Fig. 271 the effective resistance of the load is $L^2\omega^2/r$ which must be equal to R_p for maximum power output. This is not the condition for maximum efficiency, but is the condition for maximum power output under a given set of conditions. As a matter of fact the efficiency under these conditions is 50 per cent.

346. Obtaining grid bias by means of resistance leak.—During the part of a cycle when the grid is positive (shaded area in Fig. 272) the grid draws current. When the grid is negative it takes no current. There is in the grid circuit, then, an average grid current. This current can be made to flow through a resistance and, as in the case of a detector tube, be used to maintain the grid at a negative potential with respect to the filament. Since grid current flows it follows that some power must be wasted in the grid circuit. This power is that wasted in the grid leak, usually of the order of 5000 to 10,000 ohms, and that wasted in the grid-filament resistance. This power must be supplied by the plate battery, and lowers the overall efficiency of the tube and circuit. If the current is permitted to become very high the power dissipated in the grid may become too great for the tube to handle, and breakdown results.

In high-frequency circuits, the grid-filament capacity has low enough reactance to conduct currents of considerable magnitude. These currents must flow through the grid-filament input resistance, and this represents another loss in power which must be kept below the value that is safe for the tube. A choke coil placed near the grid leak is one way to prevent unwanted oscillations occurring at a very high frequency partially determined by the tube capacities. (See Fig. 273.)

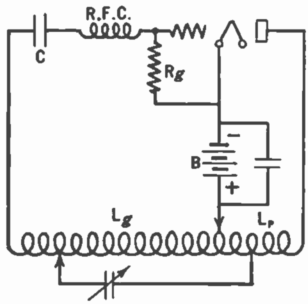


FIG. 273. — Hartley oscillator; grid current through R_g provides negative bias for the grid; choke *R.F.C.* prevents high-frequency oscillations.

Problem 7–17. The grid bias required on a tube is 60 volts. If the bias resistance is 5000 ohms, what must be the grid current flowing? What power must the resistor be capable of dissipating as heat?

347. Practical circuits.—There are a number of circuits which with an amplifying tube will produce oscillations, that is, transform d.-c. power from a battery or plate supply system into a.-c. power. All that is necessary is a tube that will amplify, coupling between input and output of proper phase and magnitude, and of course the filament, grid and plate power.

The coupling between input and output can be through inductance, mutual inductance, capacity, or resistance, or through the plate-grid capacity of the tube itself.

348. Hartley oscillator.—The simplest circuit, that is, the circuit which requires the least amount of apparatus, is the Hartley. It requires only a coil with taps on it, a tuning condenser, the tube and power supply. The coupling between plate and grid circuit is through mutual inductance between the two parts of the tuning coil, L_p and L_g. If the tuning condenser is placed across the plate circuit only, the circuit is exactly the same as Fig. 271. The circuit is given in Fig. 273. A.-c. currents flowing in the plate coil, L_p, induce voltages in L_g which are applied to the grid, amplified, and again applied to the plate coil. These voltages are 180° out of phase because they are at opposite ends of the coil with the center grounded to the filament. In Fig. 273 the plate battery is placed in the center-tap so that it is at ground potential. In Fig. 271 the plate battery, which has a high capacity with respect to ground, is connected to the plate and thereby partially shorts the plate of the tube so far as radio frequencies are concerned. A better way is to use the circuit in Fig. 273. Since this circuit would make the grid and plate at the same positive potential, which is the potential of the B battery, the grid is isolated so far as d.c. is concerned by the blocking condenser. The proper bias voltage is secured through a grid leak to the filament or through a choke and *C* battery as in Fig. 274. The feed-back between grid and plate circuits is adjusted by varying the center filament tap. If more turns are in the plate coil a greater voltage will be induced into the grid coil ($L_g \omega I$) and so greater feed-back from plate to grid circuits would result.

For covering a wide range of frequencies with plug-in coils, the Hartley oscillator is useful. It is used most frequently in laboratory apparatus.

349. Shunt-feeding oscillators.—In Fig. 273 the B battery is in series with the plate coil. The terminals of the condenser, so far as d.c. is concerned, are at the same voltage as the B battery and of course this is exceedingly dangerous since the operator, who is standing on the ground to which minus B is attached, may touch the plates or shaft of the condenser, and thereby provide a short within himself for the full plate voltage.

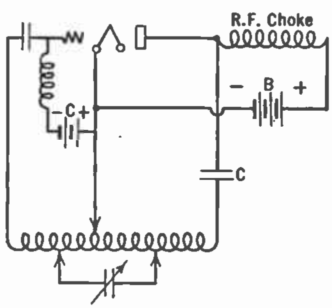


FIG. 274.—Shunt-feed Hartley oscillator keeps high d.-c. voltage from tuning condenser plates.

To prevent trouble of this kind the plate voltage may be fed into the tube through a separate path by means of a choke coil and blocking condenser as shown in Fig. 274. Now the d.-c. potential of the plate is kept from the tuning coil and condenser by the condenser *C*. The reactance of the condenser must be low compared with the reactance of the choke at the desired frequency so that the plate coil is not short-circuited so far as r.f. is concerned.

In a similar manner the use of a blocking condenser in the grid circuit and a choke for feeding the *C* bias into the grid is a shunt or parallel feed method of separating the d.-c. and a.-c. currents and voltages. In Fig. 274 there are no d.-c. currents or voltages on the tuning circuits, nor a.-c. currents in the C or B batteries.

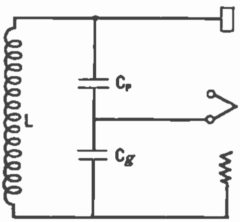


FIG. 275.—Fundamental Colpitts circuit.

350. Other oscillating circuits.—If the inductances and condensers in Fig. 273 are interchanged, as in Fig. 275, we have the Colpitts circuits, a typical arrangement of which is shown in Fig. 276. In amateur practice the tuning condensers are on the same shaft which is grounded to the filament. The chief advantage of this circuit lies in the small a.c. potentials across the chokes.

In Fig. 277 is the tuned-plate-tuned-grid circuit. Input-output coupling is provided by the tube's grid-plate capacity—one of the few places in radio circuits where this unwanted and obnoxious capacity is put to use. Whenever the plate circuit is tuned so that it is sufficiently positive in reactance, the system will oscillate, and it is not when the plate and grid are both tuned to the same frequency as many amateurs think. In this case the plate inductance must always be somewhat greater than that necessary to resonate the tuning condenser to the frequency at which the grid circuit is tuned. Tuning the plate circuit to a high wavelength, or lower frequency than the grid, is the same thing said in other words. This circuit has somewhat greater frequency stability because of the high-impedance plate load. In practice the *C* bias would not be shunt fed.

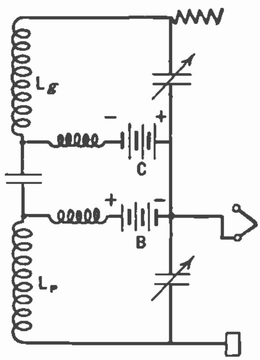


FIG. 276.—Practical Colpitts circuit.

A resistance feed-back that is employed in laboratory oscillations is shown in Fig. 278. As in all such circuits, the grid excitation is greatest when the largest coupling between grid and plate coils is used. Then the plate circuit variations are considerable in magnitude, they use curved parts of the characteristic, and harmonics are generated. In a laboratory oscillator where harmonic production is to be kept to a minimum, the coupling between input and output circuits should be adjusted at each frequency to the least possible amount that will insure stable oscillations. The resistance feed-back method is useful in such oscillators because of the mechanical ease of adjusting the feed-back voltage.

In Fig. 278 the coils are iron core inductances and the currents generated are at audio frequencies.

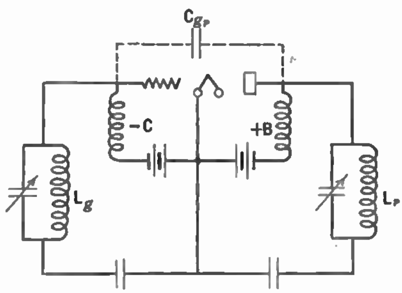


FIG. 277.—In the tuned-plate tuned-grid circuit C_{gp} acts as the feed-back agency.

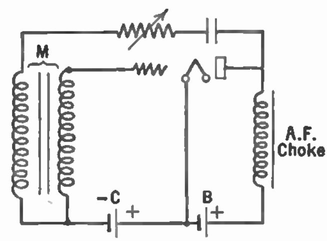


FIG. 278.—Circuit often used in low (audio) frequency oscillators.

351. Adjusting the oscillator.—When the oscillator is used to deliver power to an antenna it is desirable to attain the adjustment which will either deliver maximum output, or secure maximum efficiency so that greater inputs may be used. The tuned-plate tuned-grid circuit has no adjustments. The operator tunes either the plate or grid circuits until the tube oscillates and there is nothing else he can do. In fact, if he does not tune the circuit to an oscillating condition the plate current may be very high.

In the Hartley circuit, however, it is possible to move the center filament tap and so to get some control over the strength of oscillations, the feed-back voltage, etc. In Fig. 279 is illustrated the result of varying the filament tap on a simple 40-meter oscillator of the Hartley type. The curve gives the plate current, I_p, the current, I_a, into an antenna coupled to the plate coil, and the ratio of antenna current to plate current as some measure of the efficiency of the circuit. What is wanted, from an amateur's standpoint, is much antenna current and little plate current. The greater is this ratio, the greater is the efficiency of his circuit.

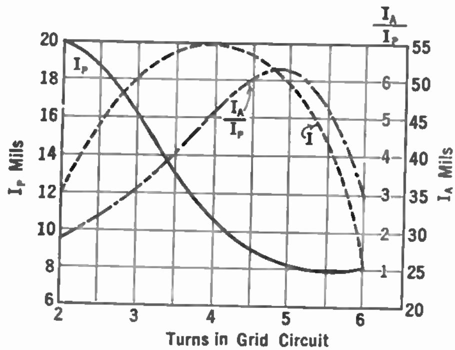


Fig. 279.—Effect of varying grid turns, thereby changing excitation.

The connection between plate voltage and oscillating current is shown by Fig. 280 to be linear. The grid bias measured across a 5000-ohm resistor is plotted too. The tube was a UX-210 oscillating at 1225 meters in a tuned plate circuit, Fig. 271. The effect of changing the C bias resistor of a tube in the tuned-grid-tuned-plate circuit is shown by Fig. 281.

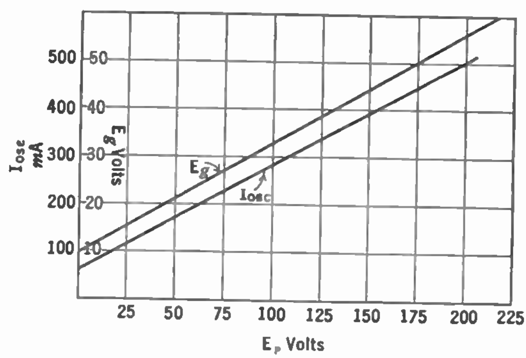


Fig. 280.—Relation between plate voltage and oscillatory current and grid bias.

352. Frequency stability. — When such circuits are used for transmission or for laboratory measurements where a constant frequency output is desired, complications set in. The frequency of such circuits is determined chiefly by the inductance and the condenser across it. This condenser is also shunted by the input capacity of the tube. This input capacity is a function of the plate load and the grid-plate capacity of the tube. In fact the input capacity C_i as a function of the load and this grid-plate capacity is

$$C_i = C_{gf} + C_{gp}\left(\frac{\mu R_o}{R_o + R_p} + 1\right),$$

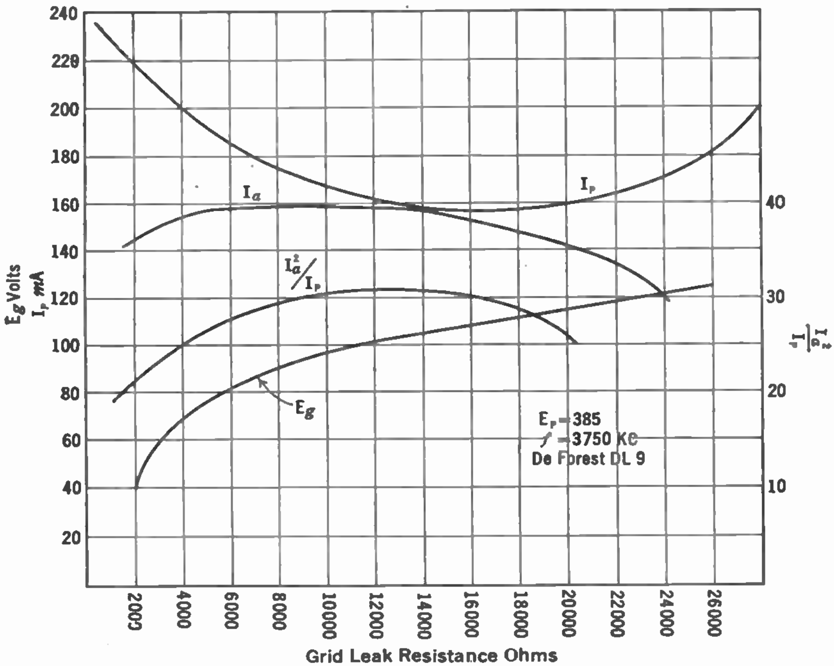


FIG. 281.—Effect of varving grid leak resistance.

which shows that any change in the plate resistance R_p of the tube or in the grid-plate capacity of the tube, or the output load R_o produces a change in the grid-filament capacity which may have a share in determining the frequency to which the system oscillates. Changes in filament temperature, in C bias, or in plate voltage will affect the plate resistance of the tube and change its relation to the load resistance. Such changes produce a change in frequency of the oscillator's output. The smaller is the plate load, the larger the grid-plate capacity; the greater the plate resistance of the tube, the more will the generated frequency depend upon these factors.

One way to lessen this difficulty is to make the fixed input capacity of the tube which is across the tuned circuit so large compared to its normal grid-filament capacity that changes in the latter are unimportant. Thus, shunting a fairly large capacity directly across the grid and filament will increase the total effective input capacity so that small changes in the internal capacity of the tube will have little effect upon the tuning.

Another method is to make the tuning condenser very large, in other words to use a high-capacity-low-inductance circuit. Such circuits have large circulating currents in them, but small voltages, and at times are very inefficient.

353. Master oscillator systems.—Where large amounts of power are to be transferred to an antenna, or other load, the place of the single oscillating tube is taken by a smaller oscillator and a large power amplifier driven by this tube. In other words we have a self-excited oscillator and a separately excited amplifier. If the oscillator is carefully stabilized against frequency changes, the output of the amplifier will be constant too. Changes in the load (the antenna for example) into which the amplifier works will not affect the frequency at which the oscillator is generating.

Such a system is called a " master oscillator, power amplifier " system and is used in all broadcasting stations and all transmitters of appreciable power. The oscillator can be of any conventional type; the amplifier may be a single tube, may be several in parallel, or push-pull, or several in cascade, just as in audio amplifiers. The chief difference lies in the fact that considerable power is being handled and so the circuits are made up of heavy conductors and use large water-cooled tubes which may use plate voltages as high as 10,000 volts and several amperes of plate current. (See Fig. 282.)

The amplifiers may be neutralized—usually are—or they may use screen-grid power-amplifying tubes which have very low grid-plate capacities and so need no neutralization.

A simple master oscillator system is shown in Fig. 283. Here the power amplifier is a 50-watt tube which is to be operated at 50 per cent efficiency. That is, 50 watts go into the load, and 50 into the tube. If the plate voltage is 1000 and the instantaneous voltage on the plate is to be just reduced to zero once in each cycle, the peak a.-c. voltage will be 1000. If the μ of the tube is 25, the a.-c. grid voltage must be at least 40, and if the inductance of the oscillator plate circuit is known it is a simple matter to calculate the current that must flow through it to set up a voltage of 40 with which to drive the following tube.

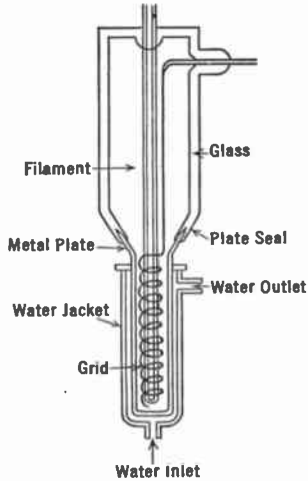


FIG. 282.—Construction of water-cooled tube.

354. Crystal control apparatus.—A quartz crystal cut with proper respect to its optical axis has the ability to control the frequency of an oscillator to a remarkable degree. When such a slab of quartz is compressed mechanically, an electrical difference of

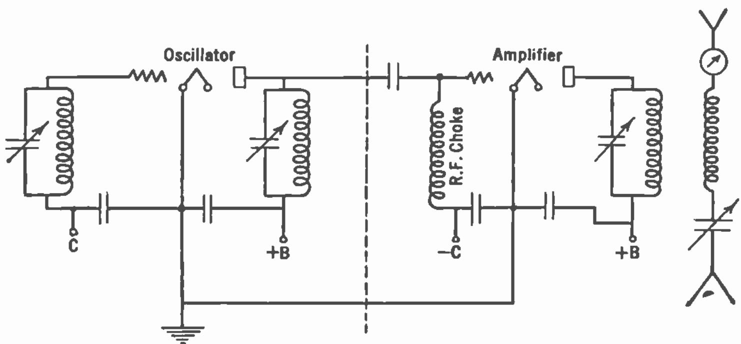


FIG. 283.—Master oscillator-power amplifier transmitting circuit.

potential is generated across its two faces. Conversely, when such a difference of potential is set up across its faces, it tends to change its size. It may be thought of as a tuned circuit whose frequency is fixed by the dimensions of the crystal. The thicker it is the longer the wavelength to which it resonates. The manner in which the crystal is cut is of utmost importance; if it is cut in one manner, the relation between frequency and thickness is 2.64 meters per thousandth inch, and if cut in another, the relation is 3.87 meters per thousandth inch. A crystal quartz plate 1.0 millimeter thick will resonate to 2860 kc.

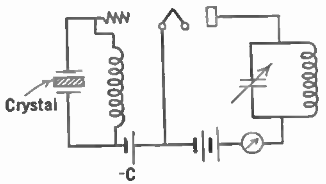


FIG. 284.—Place of crystal in oscillator circuit.

If connected as in Fig. 284 it takes the place of the tuned grid coil in the tuned-plate tuned-grid circuit. For several degrees of the plate tuning condenser the output frequency is that of the crystal, and so changes in plate resistance of the tube, battery voltages, etc., will have a relatively small effect on controlling the frequency at which the circuit oscillates.

The frequency at which the crystal resonates depends to some extent upon the temperature of the crystal. In the best transmitting stations, the crystal plate is maintained at constant temperature by complicated thermostats and electrical heating coils. Then the frequency of a broadcasting station can be maintained within 50 cycles of its assigned frequency, say 1000 kc. This is an accuracy of 50 parts in one million of 0.005 per cent. The effect of temperature on a small oscillator may be seen in Fig. 285, and the effect of changes in plate voltage on the oscillator tube in Fig. 286.

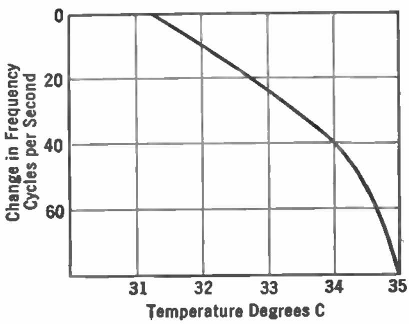


FIG. 285.—Effect of temperature on frequency.

355. Frequency doublers.—The amount of power a crystal can control is limited. If the crystal is called upon to handle too much power it is liable to crack. The power that can be controlled is about the output of a 5-watt tube on broadcast and higher frequencies where the plate becomes very thin, and certainly not over 50 watts can be controlled with safety.

The crystal oscillator is followed by amplifier stages until the required amount of power is ready for the antenna. These stages of amplification can be single tubes neutralized if necessary; they may be push-pull tubes, they may be tubes in parallel. The purpose of each succeeding tube is to provide a voltage at the required frequency and of the required magnitude which may be used to drive the grid of the next tube.

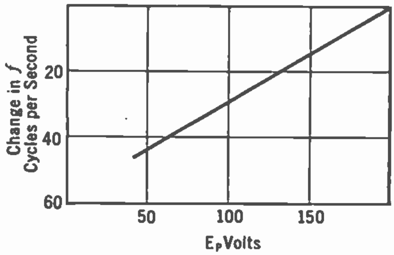


FIG. 286.—Effect on frequency of changes in plate voltage of a crystal-controlled oscillator.

For high frequencies the problem of crystal breakage, and from oscillation in the amplifier stages, becomes serious. The method usually followed is to use a fairly large crystal which drives an oscillator. Let us suppose the antenna is tuned to 40 meters. The crystal may oscillate at 160 meters. The tube is so biased that it generates a strong second harmonic, or 80 meters. This 80-meter output is fed into the grid of the next tube, whose output may be tuned to the second harmonic of 80 meters, or 40 meters. Neither of these amplifiers shows much tendency to oscillate because of the fact that the input and output circuits are tuned to different frequencies. By proper values of C bias a strong harmonic can be secured and the final power tube driven by a 40-meter voltage.

Such transmitters can operate from either a.c. or d.c. If they are to be used for telephone transmission, broadcasting, for example, pure d.c. is necessary. For code transmission some slight ripple in the output is probably desirable if the signals are to be copied by ear at the receiving station. If they are to operate a relay and mechanical apparatus, the character of the signal may be adapted to the receiving apparatus, or ignored entirely. A "frequency doubler" is shown in Fig. 287.

356. Self-rectified transmitters.—When a.-c. voltages are applied to an oscillator tube, it rectifies them and plate current flows during the time the plate is positive. In other words, the circuit oscillates half the time. On the negative half-cycles the circuit is non-operative. The signal as it is heard at the receiving station has a characteristic note depending upon the frequency of the transmitter power supply, and the adjustments at the transmitter. A transmitter of this type is called a self-rectified circuit because the tube furnishes its own plate voltage by rectifying an a.-c. wave. Two such tubes may be used in push-pull or "back to back" to rectify and oscillate on opposite halves of the a.-c. cycle. The transmitted note then will have double the frequency of a single-wave rectified transmitter. A circuit of this kind is shown in Fig. 288.

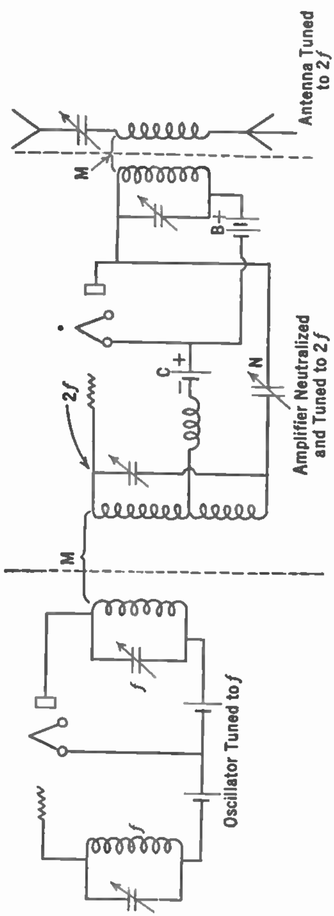


Fig. 287.—A frequency doubler. A second harmonic (2f) voltage in the plate circuit of the oscillator drives the following amplifier.

Such transmitters take up more room in the ether than is desirable, and even though controlled by crystal seem to vary from their assigned channel because of variations in the audio-frequency modulations. A transmitter using 500-cycle source of plate voltage will require a channel width of 1000 cycles when holding its key down. Ether space required for it depends upon adjustments of several circuit factors.

357. Adjusting the plate load to the tube.—The condition for maximum output of a tube with a given amount of power to be taken from the plate battery is that the load into which the tube works is equal to the plate resistance of the tube. The load is the resistance of the tuned circuit. Now the value of L and C are more or less fixed in this circuit, which leaves the series resistance as the only independent variable factor. Suppose, for example, we desire to generate oscillations 1000 kc. in frequency in a tuned circuit. This determines the frequency. We can choose L and then C is

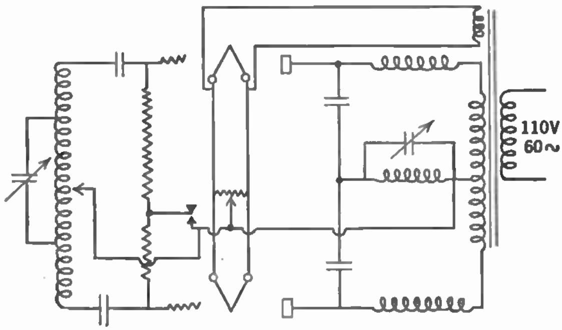


Fig. 288.—Full-wave self-rectified oscillator operated entirely from a.c.

fixed; we cannot change their ratio which determines the effective resistance, L/Cr. What can be done so that the tube generates the maximum amount of power in the tuned circuit?

If the proportion of the entire tuned circuit across which the tube is connected is varied the impedance into which the tube works will be stepped down; and by properly choosing the plate tap in Fig. 289 the proper load will be presented for the tube to work into so that the maximum power will be delivered. The inductance of the tuned circuit may be looked upon as a transformer which couples the tube to its load, usually an antenna.

358. Plate current when oscillator is connected to antenna.—An antenna-counterpoise system is usually connected to the power tube through an inductance which is a part of the tuned antenna system. This antenna system is tuned to resonance with the tuned circuit. If the oscillator is adjusted to its proper frequency by varying the inductance or capacity of its tuned circuit, and the plate tap is then adjusted for maximum power output, the antenna coupling inductance may be brought near the tuned circuit inductance. If then, the tuning capacity of the antenna is varied through resonance with the transmitter, current will begin to flow into the antenna, and the plate current of the tube will probably increase because the battery must now furnish the power taken by the antenna as well as the power lost in the tuned circuit. Closer coupling will induce a greater voltage in the antenna, more antenna current will flow, the plate current will increase, and greater power

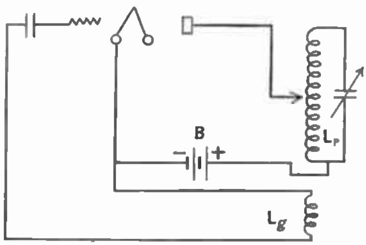


FIG. 289.—Maximum power is obtained by adjusting tap until tube works into its own impedance.

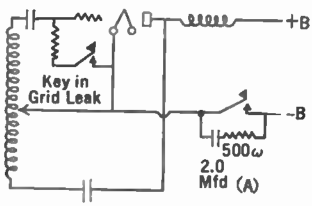


FIG. 290.—Two methods of keying transmitter. Note "thump" filter in $-B$ lead.

will be radiated. Since the antenna is being coupled to the tuned circuit its resistance is being reflected into the plate circuit and some readjustment of the plate tap must be made. This may change the frequency slightly, and so all four variable factors—coupling, plate tap, and tuning, and tuned circuit capacity—must be adjusted until the maximum power is transferred to the antenna at the required frequency.

A rough idea of the power being radiated may be estimated in the following manner. Suppose the plate current without the antenna is 100 milliamperes and the plate voltage is 1000 volts. This represents a power input to the tube of 100 watts. Now suppose the antenna is coupled to it, and the plate current increases to 150 ma. The power is now 150 watts. The difference between 150 and 100 watts, 50 watts, may be assumed as going into the antenna. If the antenna current is measured, a rough estimate of the antenna resistance may be had. The method is not at all accurate unless a sine wave is being radiated and then only approximately.

359. Keying a transmitter.—There are several methods of modulating the oscillations of a transmitter so that they may convey intelligence from one operator to another. The tube may be caused to cease oscillations, the antenna circuit may be broken or closed or the frequency to which the oscillator is tuned may be changed in accordance with the manipulations of the key. A key placed in the plate voltage supply (Fig. 291) will cut off the power. This method is not successful with well-filtered systems because of

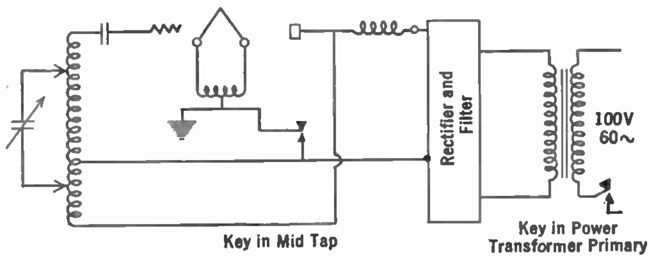


FIG. 291.—Keying in "center tap" or in transformer primary.

the time taken to completely discharge the condensers. An alternative place for the key is the grid circuit, as in Fig. 288 or 290. If the grid leak or the C bias lead is opened by the key, there will be no path for the electrons trapped on the grid to escape. The grid will them assume a large negative voltage which will reduce the plate current to such low value that oscillations cease.

If the key is placed in the plate lead it must break the full power to the tube, and its contacts must be able to handle the current without heating and without breakdown from the voltage drop across the key as it is opening.

The voltages and currents in the grid circuit are much lower. Both of these methods of starting and stopping the oscillations are abrupt and provide the nearby ether with profound shocks known among the amateur fraternity as "key thumps" and cordially hated by listeners to other transmissions. Various thump filters have been devised to start and stop the oscillations in the tube less abruptly. One method is to let the tube oscillate feebly during the periods the key is up by placing a high resistance across the key contacts. Another is to place a resistance, capacity, and inductance across the key contacts. The condenser charges and discharges slowly and prevents the abrupt opening of the plate power circuit. The inductance (about 0.5 to 2 henrys) slows up the start of oscillatons.

Keying can be accomplished as in Fig. 291 but generally the break is made *between* the filament and the connection to minus B, which is also attached to the grid. In other words the filament only is cut loose. This is called "keying in the common lead" and is quite common.

360. Too close coupling to antenna.—If the closed circuit is properly tuned and the antenna coupled to it, it may be found that the emitted wave is no longer of the desired frequency or that the tube refuses to oscillate or that as the antenna tuning condenser is varied two maxima of antenna current will be noted. Such trouble will occur whenever both circuits are tuned to the same frequency and then too closely coupled or when the two circuits have slightly different frequencies and are coupled together.

Good amateur practice dictates that the antenna circuit should be tuned as closely as possible to the closed circuit frequency by watching the antenna ammeter. Then the coupling is reduced or the circuit detuned until the antenna meter reads about 75 per cent of its maximum reading under any adjustment. Then there is little likelihood that the transmitter will suddenly decide to transmit on a frequency to which the receiver is not tuned. When the antenna tuning condenser is varied, with such loose coupling between antenna and tuned circuit, there will be but a single sharp resonance peak. There will be no danger that the frequency of transmission will jump from one peak to another, and thereby clutter up the ether with unintelligent dots and dashes.

361. Methods of connecting oscillator to antenna.—It is possible for the inductance and capacity of the antenna-counterpoise system to be part of the tuned circuit, and if so, the greatest amount of energy transfer will take place from tube to antenna. Modern methods, however, involve coupling the antenna to the oscillator through a "tank circuit," which the tuned circuit is usually called. Whatever harmonics exist in this circuit find poor coupling to the antenna and are inhibited in their voyage from the transmitter to the ether.

When the antenna-counterpoise is series tuned, it is done so to attain a maximum of current in it. On short waves the antenna is somewhat larger than one whose natural wavelength is the wavelength of transmission. This wavelength is reduced by means of the series condenser.

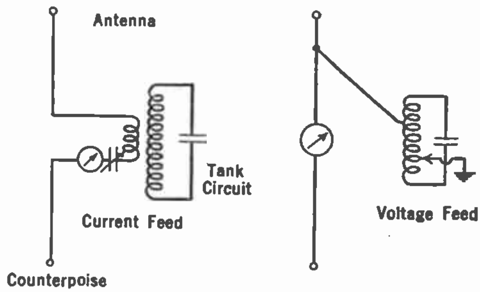


Fig. 292.—Current feed and voltage feed antenna circuits.

It is possible to put power into the antenna by what is known as the "voltage feed" method which consists in attaching one end of a wire to some high-voltage part of the tube's oscillatory circuit and the other end of the wire to some high-voltage part of the antenna. This provides sufficient coupling between transmitter and antenna to excite the latter. (See Fig. 292.)

362. Feeding power through transmission line.—Oftentimes it is impossible to put the antenna in a clear location near the transmitting apparatus. It is then possible to feed power to the antenna through a transmission line, as in Fig. 293, which is at low potential and not tuned to the frequency at which radiation is to occur. The resistance of this line is low at this frequency, little current flows in it, little power is lost in it, and the power is finally put into the antenna which may be located at some advantageous position. Transformers at the ends of this line couple it to the transmitter and to the antenna if the line is longer than ⅛ wavelength.

363. Modulation.—A transmitter may be designed either for code or voice transmission. More apparatus is required for the latter means of communication. In addition to the oscillator tubes and amplifiers which may finally feed power into the antenna, there must be a modulating system. One method is to put the audio voltage variations into the grid circuit of the oscillator. These variations are, then, superimposed upon the a.-c. plate current and so the output into the antenna is varied at the audio-frequency rate.

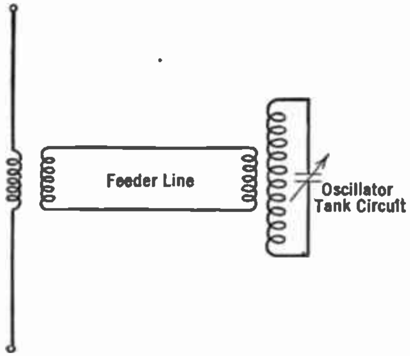


FIG. 293.—Energizing an antenna by means of a feeder line which does not radiate.

The system most frequently used is known as the Heising or constant-current system. In it, the plate voltage to an oscillator, whose frequency is the carrier or high frequency, is varied by the audio-frequency modulating voltages. Since the oscillating current and hence the antenna current is proportional to the plate voltage (Fig. 280), this current will vary with the audio variations.

Consider Fig. 294, in which the reactance of the choke L is high at all audio frequencies compared to the two resistances. The resistance R_m is the resistance of what later will be seen to be the modulator tube, which is simply a power amplifier operating at audio frequencies. The resistance R_o is the resistance of the oscillator tube. Suppose the resistance of R_m is caused to vary at some audio rate. The current taken from the B battery will not vary at this rate because of the large choking effect of the inductance L. The total current, then, from the battery is constant. If the resistance of the modulator tube, R_m, increases, less current will be taken by it and more can be taken by the oscillator tube. On the next half-cycle, the resistance

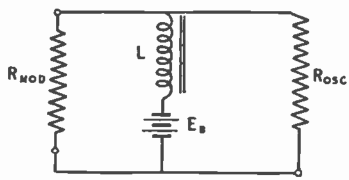


FIG. 294.—Equivalent of Heising modulation system

of the modulator tube decreases and more current will be taken by it. The current taken by the oscillator then must decrease.

If the variations in resistance of the modulator tube are at some audio frequency, say 1000 cycles, the current taken by the oscillator will vary at this rate too—which is another way of stating that the r.-f. currents generated by the oscillator and transferred to the antenna will be modulated at the rate of the audio variations in the modulator circuit.

The actual circuit is shown in Fig. 295. When the r.-f. output of the oscillator is completely modulated, it looks as in Fig. 296

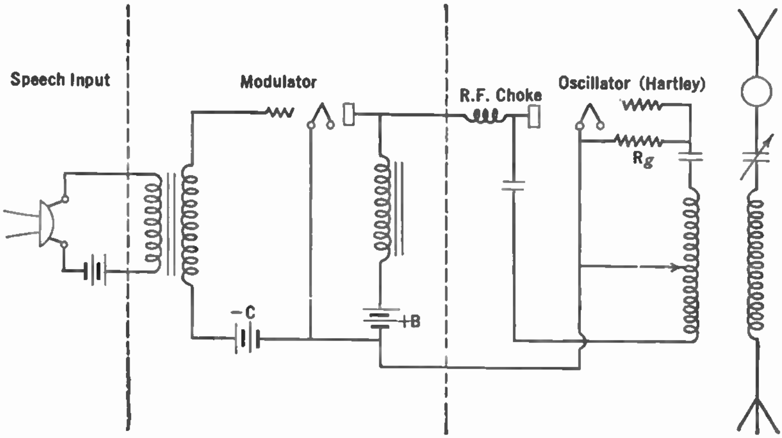


FIG. 295.—Practical modulated oscillator circuit.

(taken from Heising, Proc. I.R.E., August, 1921), and the power in the antenna is 1.5 times as great as when no modulation occurs. The antenna current meter will read the effective value of the current, or the square root of the power, and so will increase about 20 per cent when the wave is completely modulated. (The square root of 1.5 is 1.226, which is 22.6 per cent greater than 1.0.)

364. Amount of power required for modulation.—It used to be standard practice to use a modulator tube of the same rating as the oscillator tube. That is, if the oscillator was a 50-watt tube, the modulator was a 50-watt tube. Nowadays, however, the modulator has considerably more power than the oscillator, for the following reason. When the tube circuit oscillates a considerable part of the energy from the plate battery is taken from the plate of the tube and used up in the tuned circuit or the antenna as the case may be. In other words a 50-watt tube may actually take 100 watts from the plate battery. Let us suppose it takes 100 watts. Now to completely modulate the oscillator means that once in each audio cycle the voltage on the plate of the oscillator will be reduced to zero, or very near it, and once in each cycle the voltage on the tube will be doubled. This means that the modulator

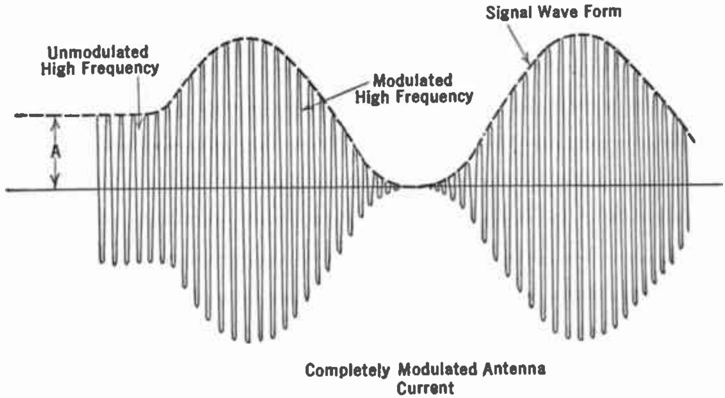


FIG. 296.—A radio frequency wave before and after complete modulation.

tube must draw as much power as the oscillator, but it cannot because its plate would burn up—it is not oscillating. It must be biased so that the no-audio-signal input condition leaves the power wasted on the plate not over 50 watts. When the microphone is spoken into the steady plate current will change, showing that it was not acting as a distortionless amplifier.

The solution is to use more modulator tubes so that the combined plate current times the plate voltage is equal in power to that taken by the oscillator. Even then complete modulation of the oscillator is impossible because such a condition would imply that the plate voltage on the modulator would be reduced to zero at some instants. This is impossible without severe distortion.

The result is that modern equipment operates the modulator tubes at higher voltages than the oscillator.

There is another difficulty in the modulation procedure. The antenna current under 100 per cent modulation indicates that 50 per cent more power is being supplied. This power must come from the modulator. In addition to supplying to the oscillator peak voltages equal to the steady voltage of the oscillator B battery, the modulator must supply the additional 50 per cent of power. Since the modulator, acting as an amplifier, cannot be very efficient, a large battery of tubes is required in the modulating system.

365. Modulation at low power.—Suppose, however, we modulate the output of a small tube and amplify it. We shall save on modulation equipment, because we can modulate a 5-watt tube, say with a 50-watt tube, and when small quantities of power are to be used efficiency does not matter. The succeeding power amplifiers, however, must each carry the additional 50 per cent increase in power, if the wave is to be completely modulated, and so little has been gained. It is a problem of whether to build a large modulating equipment acting at audio frequencies or large radio amplifier equipment.

366. Distortion at receiver due to complete modulation.—Detectors work according to a square law at low signal inputs, say up to about 0.2 volt. Because of this square law detection, distortion results in the receiver. When the wave is completely modulated, there will be a second harmonic current in the output of the detector of 25 per cent of the fundamental. With a good amplifier, and loud speaker, this distortion is evident to a critical ear.

Let us look at Fig. 297. This represents the relation between r.-f. input and a.-f. output from a theoretical detector operating according to a square law. Since modulation can be thought of as merely changing the r.-f. signal amplitude at an audio rate, let us suppose an average value of r.-f. signal is 3 volts, and that the wave is completely modulated. This means that the peak value will be 3 volts varying about an average value of 3 volts. In other words at one instant the voltage on the input to the detector will be

6 volts and at another will be zero volts. The corresponding a.-f. output will be 36 and 0 volts. This corresponds, as shown in Fig. 297, to a wave having a maximum value of 36 volts in one direction, 0 in the other, or a mean value of 18 volts.

Now suppose the modulation is only 50 per cent producing an r.-f. wave that varies from 1.5 to 4.5 volts, which in turn produces an audio wave which varies from 20.25 volts in one direction to 2.25 in another, or an average value of 9 volts. In other words, doubling the modulation percentage doubles the average value of the a.-f. output. Thus the audio-frequency output from such a detector may depend upon the square of the r.-f. input, but it depends upon the first power of the modulation.

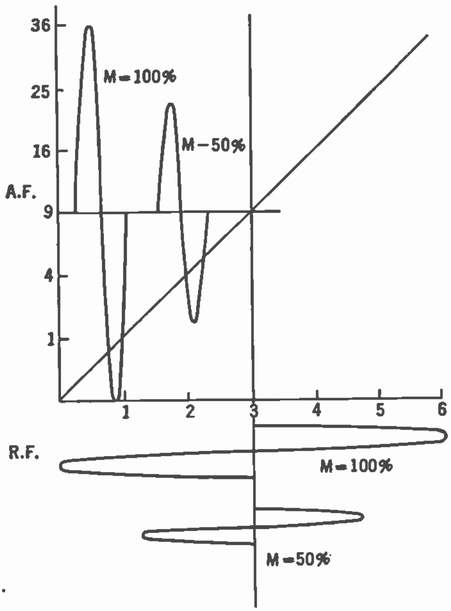


FIG. 297.—In a square law detector the *A.F.* output is proportional to the square of the *R.F.* input.

In Section 186 we determined the percentage of harmonic distortion that occurred in an amplifier when it worked over a curved characteristic. Let us apply the same procedure to the detector case and see what it brings. Increasing the r.-f. voltage a given amount produces a different value of a.f. than decreasing the r.f. the same amount does. In other words, distortion results. The wave form of the output looks like Fig. 298.

The expression for percentage second harmonic is

$$\frac{\frac{1}{2}(I_{max} + I_{min}) - I_{av}}{I_{max} - I_{min}}$$

and applying it to the two cases of 100 per cent and 50 per cent modulation we get

For 100 per cent modulation,

$$\text{distortion} = \frac{\frac{1}{2}(36 + 0) - 9}{36} = \frac{1}{4} \text{ or 25 per cent;}$$

and

For 50 per cent modulation,

$$\text{distortion} = \frac{\frac{1}{2}(20.25 + 2.25) - 9}{20.25 - 2.25} = \frac{1}{8} \text{ or 12.5 per cent.}$$

All of this proves that doubling the modulation doubles the percentage of distortion. This is the disadvantage of the square law detector; the distortion arising from its use prohibits large-percentage modulations. Low degrees of modulation mean waste of power.

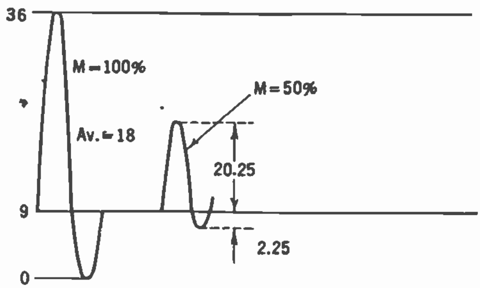


FIG. 298.—Distortion arising from square law detection.

When linear detectors or demodulators are used, the percentage of modulation at the transmitter can be increased without increase of distortion taking place in the detector. At the same time the increase in modulation will increase the detector output. Since the detector output is roughly proportional to the product of the modulation and the r.-f. carrier, increasing the modulation has the same effect as increasing the power of the transmitter, and to provide the same service at a given distance, increasing the modulation, can be accompanied by a decrease in r.-f. power. Since the distance, over which two stations interfere (produce beat interference) depends upon the carrier power, any decrease in carrier power effectively increases the number of stations that can operate in a given area and on a given frequency. Since the noise at the receiver is proportional to the carrier, increasing the modulation without increasing the carrier improves the signal to noise (static, etc.) ratio by about four to one, and so the carrier power could be reduced still more and still maintain the same service. The modern tendency is toward greater modulation—approaching 100 per cent on peaks and averaging perhaps 50 per cent—and greater carrier power as well.

Linear detection has the added advantage that undesired signals weaker than the desired signals are wiped out by the latter. (Radio Broadcast November, 1929, F. E. Terman.)

CHAPTER XVIII

ANTENNAS, TRANSMISSION

Now that we have generated oscillations and induced radio-frequency currents in an antenna, how it is that these currents convey intelligence to a receiver perhaps thousands of miles away? What is the nature of this process? What is the nature of the invisible and often unpredictable medium between transmitter and receiver?

367. Radiation resistance.—Let us suppose that two wires about 30 feet long and about a foot apart are coupled to a 40-meter transmitter through any of the familiar coupling methods, perhaps by means of a coupling coil as in Fig. 299. The current into this double-wire system will rise to a maximum when the varying tuning condenser makes the product of L and C equal to the product of L and C of the oscillator. Suppose this current is 1 ampere. Now let us separate the ends of the two wires farther and farther until finally they are stretched out straight. More and more power will be required from the plate battery to maintain a constant value of current in the wires.

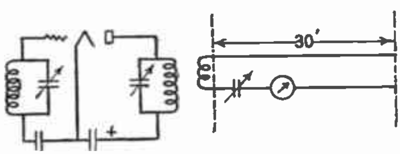


FIG. 299.—Experimental diagram to demonstrate existence of radiation resistance.

At the same time we shall note that the capacity and inductance have changed somewhat so that some minor changes must be made in the tuning condenser to keep the wires in resonance with the oscillator—but these changes cannot account for the greater power required from the battery to maintain the same current in the wires. In the first place, the changes in capacity and inductance are balanced out each time by readjusting the tuning condenser to resonance. Then there is only resistance to impede the flow of current. Every time the reactances have been balanced against each other. Clearly the resistance of the wires has increased. At the same time if we installed a small receiver near the oscillator and kept moving away from it so that the signals picked up were of constant strength, we should find that the greater the power taken from the battery and hence the greater the power into the antenna, the farther away we could hear the signals.

It is apparent that if the current is still 1 ampere but twice as much power is taken from the battery to produce the 1 ampere, the resistance of the wires has doubled. The useful part of this resistance is called the **radiation resistance** of the wires, which may now be called the antenna. The power that goes into this resistance is the power that is effective in carrying intelligent communication from the transmitter to the receiver.

The total resistance of an antenna may be measured by the same method used to measure the high-frequency resistance of a coil. (Section 134.) If enough resistance is added to our 40-meter antenna system to halve the current, this added resistance is equal to the resistance already there. If the resistance is measured at several wavelengths we shall get a curve similar to that in Fig. 300 (taken from the Proceedings of the I.R.E., February, 1920, by T. Johnson, Naval Aircraft Radio). This resistance is made up of the ohmic resistance of the wires, the losses in the dielectric of the antenna capacity, the loss of energy due to radiation, and other small losses. An efficient antenna is one which has a very high radiation resistance and a low resistance of all other sorts. Then most of the power put into the antenna from the oscillator will be radiated. This method of measuring antenna resistance is fairly accurate if very loose coupling and a sensitive meter are used.

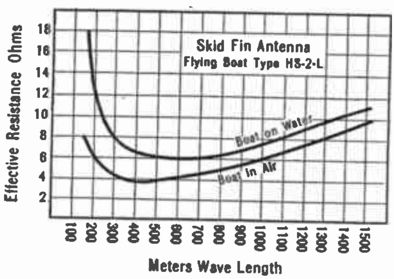


FIG. 300.—Antenna resistance.

The radiation resistance of most short-wave antennas used below the fundamental wavelength is of the order of 100 ohms and it requires a transmitter output of 100 watts to put 1 ampere into it. The current that goes into an antenna is a variable factor, and because one antenna has 1 ampere and another 2 amperes in it it may not mean that 1 is twice as good as the other. The place in the antenna-ground or antenna-counterpoise system where the current is read and the physical surroundings of the antennas may be much more important in determining the effective radiation than the current into it.

368. The radiation field.—The energy which is taken by the radiation resistance is used in setting up about the antenna a **radiation field.** This field consists of both a magnetic field and an electrostatic field. This radiation field moves away from the antenna with a speed equal to the velocity of light, and its strength at any distance is inversely proportional to the distance.

When the lines of force making up this radiation field cut a conductor such as a receiving antenna a voltage is induced in this conductor and if amplified and demodulated it becomes the received part of the communication thrust upon the ether by the transmitter.

This brief and very inadequate explanation of what happens in the ether does not state how it happens. Most radio engineers, however, are interested in the result rather than the means and so we must be satisfied with the knowledge that current into an antenna produces a radiation field about the antenna, that the intensity of this field varies inversely with the square of the distance, and that when this field cuts across a conductor to which is attached a receiving apparatus a voltage is developed which is the bearer of the messages sent out at the transmitter.

369. Calculation of the received current.—If the antenna at the transmitter is the type used on shipboard, that is, a high "flat-top," and a "down lead," and if the receiving antenna is similar in construction, the received current is a function of the transmitting current and the dimensions of the antennas, and the distance apart is

$$I_r = \frac{188\, h_s h_r I_s}{R \lambda d},$$

where h_s = the transmitting antenna height;
h_r = the receiving antenna height;
I_s = the maximum transmitting current;
R = the receiving antenna resistance;
d = the distance apart in meters;
λ = the wavelength in meters.

This formula shows that, all other conditions remaining the same, there will be more received current the shorter the wavelength, but this formula does not show the fact that short waves are absorbed more readily than long ones. The greater the height of the transmitter and receiver antenna the greater the received current. At the same time the absorption is less because of the fewer objects in the near field of the antenna and so the higher the antenna the better it is.

This formula does not include such variable factors as skip distance, sky waves, sunset effects or other vagaries of transmission on short or medium waves. It is not useful on amateur bands.

370. Types of antennas.—Antennas may take a number of shapes and sizes. Radiating systems in use in high-power long-

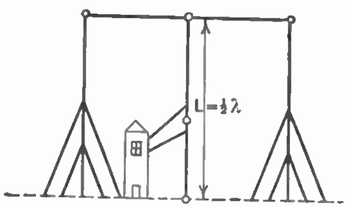


FIG. 301.—Half-wave vertical antenna.

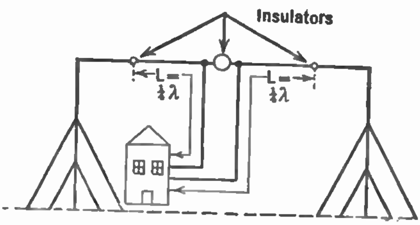


FIG. 302.—Folded half-wave antenna.

wave stations comprise a very long (one mile or more) flat-top about 400 feet high, whereas a short-wave station may have an antenna consisting of a single wire (Fig. 301), vertical or horizontal (Fig. 302), one-half wavelength long. For example, if the wave radiated is 20 meters, the total length of antenna and counterpoise wire will be 10 meters, or about 30 feet. On shipboard the "down lead" may come from the end of the horizontal part or from the center. In portable installations an umbrella type is used, that is, an insulated mast which is held up in the air by insulated wires which act as the radiating system.

The larger the antenna the more energy it will pick up, either from desired stations or from other electrical disturbances such as static. The tendency is to use large antennas for transmitting, so that a large amount of power can be put into the radiation field, and small antennas for receiving so that the ratio of signal to static will be large.

The ordinary antenna used for broadcast reception consists of a single wire more or less horizontal or vertical as the case may be, and up to a hundred feet long. Receivers are engineered with an average antenna in mind and more recent receivers, using screen-grid tubes, require no antenna at all, but pick up enough energy from a small wire or loop to obviate the unsightly and dangerous practice of installing wires on the roofs of buildings, on telephone poles and in trees.

371. Directional antennas.—For broadcasting intelligence over a wide area an antenna which transmits equally well in all directions is desirable. Such is the vertical antenna. When a station is constructed to operate with one other station only, it is a waste of power to transmit its signals in all directions. Such stations use directional antennas, that is, radiating systems which transmit better in one direction, say north-south, than they do in any other. Even then energy goes out in two directions, north and south, and the receiving station is, of course, in only one direction from the transmitter.

The loop is a directional antenna. It receives better in the direction towards which the narrow dimension points. Its pick-up ability is something like Fig. 303, in which it is pointed east-west and picks up very little energy from a north-south direction. In connection with a sensitive receiver, it may be used to determine the direction whence the signals come. It is the heart of the direction-finding stations which are situated along the coasts of the world. When a ship wants bearings, its signals are picked up by the coastal station which determines the position of its receiving loop which gives the least signal. A compass is attached to the base of the loop and the indicator then points out the bearing of the vessel. A receiving operator in another location also swings his loop on the vessel and thus two bearings will be obtained. From them the master of the ship can tell exactly where he is with regard to the coast line. The method is shown in Fig. 304.

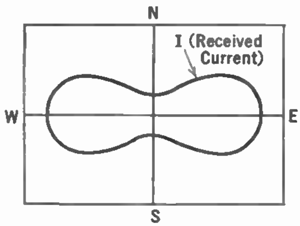


Fig. 303.—Directional effect of reception on a loop.

Other types of antenna give still greater directional effects, and those with reflectors behind them (short waves only) will transmit a narrow beam of signals in only one direction.

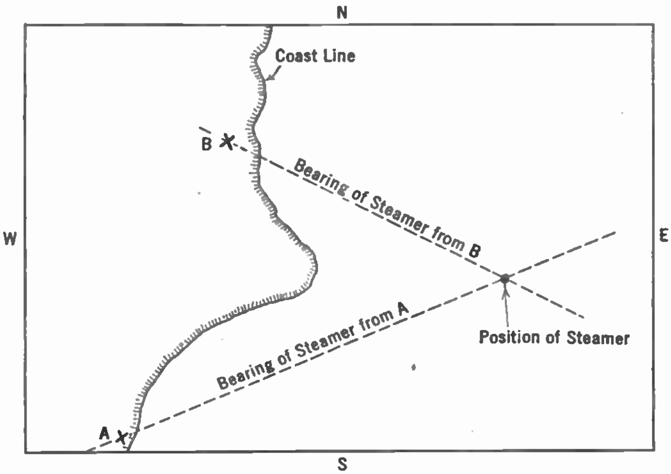


Fig. 304.—Method of plotting a ship's position by obtaining two bearings from land stations.

372. Inductance and capacity of antennas.—In Sections 136 and 137 means of measuring the capacity and inductance of an antenna were discussed. The inductance and capacity are not concentrated as they are in a coil or condenser but are distributed throughout the structure. The capacity of the antenna wire may be with respect to ground which serves as one plate of a condenser with the antenna wires as the other and the air as the dielectric, or the capacity may be with respect to some other electrical conductor, usually of the form of a **counterpoise** which is merely another antenna, that is as a rule of larger dimensions and much nearer the ground. The counterpoise is used because of its lower resistance losses than the average ground.

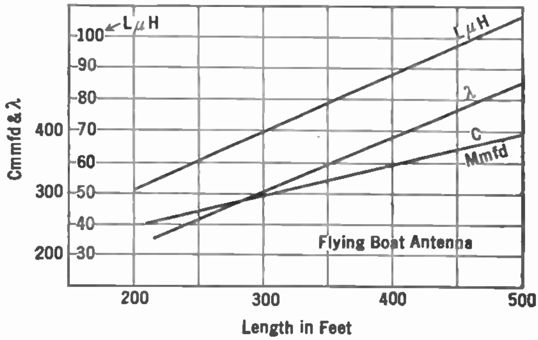


FIG. 305.—Characteristics of airplane antenna.

The inductance of most attennas is small, of the order of 50 to 100 microhenrys. The capacity of simple receiving attennas is of the order of 150–300 mfd. (See Fig. 305.)

373. Natural wavelength of antenna.—Because an antenna has both capacity and inductance it can be made to resonate to a certain frequency or wavelength. The formula for the wavelength or frequency to which an antenna resonates is the same as in any other circuit which has a capacity and inductance, that is,

$$f = \frac{1}{2\pi\sqrt{LC}}.$$

A vertical wire grounded at the lower end has a natural wavelength about 4.0 times its physical length. Thus, if the wire is 20 meters long and is grounded, its natural wavelength is about 80 meters. On the other hand, if the wire is not grounded but is considered as being two wires, an antenna and counterpoise with maximum current in the center, the natural wavelength is roughly twice the length in meters. Thus, an antenna 20 meters long (30 feet in antenna and 30 feet in counterpoise) will radiate a wave of 40 meters if not connected to the ground. This antenna is called the Hertz because it is the type used by that investigator.

The Hertz antenna can also be made to radiate on any of its harmonics. It is natural wavelength is 40 meters it will radiate at 20 meters or if excited properly by an oscillator, at 10 meters.

374. Loading an antenna.—In case an antenna does not have the required inductance to bring its wavelength to the desired value, additional concentrated inductance can be placed in the down lead and the antenna "loaded" up to the desired wavelength. Since the coil cannot radiate to any extent and since its resistance must be added to the resistance of the antenna system, loading makes the entire system inefficient. The small antenna gets poor "hold" on the ether; the higher current causes greater power loss.

375. Decreasing the wavelength of an antenna.—If the antenna is too large to tune to the desired wavelength its natural wavelength can be reduced by placing a condenser in series with it. This reduces the effective capacity and as a result reduces its wavelength. The wavelength cannot be reduced below one-half the natural wavelength. Here again, loss in power in the condenser must be subtracted from the power that would go into the radiation resistance and so the losses in the condenser must be paid for in inefficiency. Fortunately, it is possible to build a condenser whose resistance may be very low at the frequency at which it is to be worked, and so a series capacity does not add much resistance to the antenna.

376. Short-wave transmission.—Because of the fact that short waves were highly absorbed, it was thought for many years that this portion of the radio-frequency spectrum was worthless. It was largely for this reason that amateurs were permitted to operate there. No one else wanted the short waves. Strangely enough, these short waves, once thought worthless, are now being fought for by radio communication companies the world over.

The radiation field as it goes out from the antenna is absorbed by all conductors which exist in its field. According to theory, the shorter the wavelength the greater the absorption so that for waves shorter than 100 meters very little energy arrives at a receiver any distance away. Amateurs, however, discovered that these waves did arrive at much more distant points than theory permitted and a new theory had to be developed.

Waves are radiated from the antenna at all angles to the horizontal. The **ground wave** which the old theory dealt with goes near the surface; some radiation leaves the antenna at a high angle and shoots off into space. Some distance above the earth is an ionized layer which is a fairly good conductor of electrical disturbances. It therefore reflects a certain amount of the **sky wave** which returns to earth and may be received by any antenna in its path.

The ground wave is soon absorbed. The sky wave does not come down to earth in the immediate vicinity of the transmitter. Between the area covered by the ground wave and the sky wave there is a dead spot known as the **skip distance.** Signals are not received there except with the greatest difficulty and with considerable irregularity. In the daytime this skip distance is about 200 miles at 40 meters and 800 miles at 20 meters. Beyond the skip distance the signals are audible and fall off in intensity until they are again inaudible.

By properly choosing the frequency for the time of day it is possible to maintain a continuous communication with another station at any given distance. In other words, distance, time of day, and frequency are related. The table at the back of this book was collected by L. C. Young of the Naval Research Laboratory and published in *Radio Broadcast.*

It is because of the sky wave that amateurs working with less than 100 watts in an antenna are frequently able to communicate over several thousand miles on waves below 80 meters. Above 300 meters the skip distance is negligible, the sky wave is not important, except as noted in Section 377.

377. Fading.—Because the Heaviside layer, as the ionized conducting layer which about 100 miles above the earth is called, varies in height and density from moment to moment and from day to day and season to season, the reflected wave varies in intensity. This is one cause of fading. Amateurs and other workers on short waves are the ones who have to contend most with this phenomenon since it is less effective on longer waves. It is of some importance on broadcast frequencies but at lower frequencies becomes of less and less value. When the sky wave and the ground wave arrive at a receiving station out of phase with each other, the received signal will be decreased in strength. This accounts for some fading experienced on broadcast frequencies.

The automatic volume control discussed in Section 308 will do away with the effects of fading, even at its worst, if the transmitting station is powerful enough to lay down a good field strength at the receiver. The weakest signal must be 40 DB above the noise level. Then the volume control will keep this difference between noise and static by reducing both when the signal comes up. If the signal gets below the noise or equal to it, the automatic increase in sensitivity of the receiver will only bring up the noise with the signal.

378. Comparison of night and day reception.—The shorter the wavelength the greater the difference between night and day transmission and reception. On long waves there is little difference. At night signals are somewhat louder. On broadcast frequencies the difference is marked, especially in winter. Signals can be heard at night which are inaudible during the day. On short waves the skip distance becomes much greater at night. Why is this?

During the day the sun pours radiation into our atmosphere ionizing the particles which constitute it. These ionized particles absorb radiation of all kinds. Once absorbed, their energy is lost and they cannot transmit intelligence to distant receiving stations. At night this ionization ceases, the absorption of radio waves decreases and signals again reach out. The Heaviside layer of ionized particles which reflects the sky wave on the frequencies above 3000 kc. is very low in the daytime. The skip distance is not so great then as it is on a winter night when the Heaviside or reflecting layer is high, 100 miles or more above the earth.

379. Static.—Static is part of the noisy background that is sometimes of sufficient strength to interfere with the reception of signals. It is caused by natural phenomena, such as discharges of electricity between clouds at different potential or from clouds to earth. It is not the same noise that is caused by a leaky transmission line, defective power transformers, wires rubbing in trees and sparking, or other noises which come under the heading of man-made static. All of the latter noises can be eliminated. Static cannot be eliminated but its effects can be reduced.

A receiver that operates from a very small antenna will pick up less disturbing noise than a large antenna high above the earth The loop antenna which can be pointed at the desired signal, or any other directional antenna, will not pick up static or unwanted signals from other directions and will produce a greater signal to static ratio. It has the effect of reducing static.

A number of schemes have been devised to reduce the static to the level of the signal, but none has yet been made that will eliminate the static without also eliminating the signal. Both are produced by the same fundamental phenomenon—the charge and discharge of a condenser. One is produced in a broadcasting station by man, the other in the sky by nature.

Static is more bothersome during hot summer weather when the clouds are highly charged. The more sensitive one's receiver the further away the storms can be and still disturb reception. Man-made static is bothersome at all times of the year and at any time of the day or night. In the future all man-made static will be illegal, just as it is now illegal to operate an automobile without a muffler.

380. Elimination of man-made interference.—Considerable advance has been made towards the elimination of radio interference from all manner of sparking machines. The sparks must be eliminated or the electric waves they set up must be prevented from radiating much energy. If the sparks occur in a large system of wires the energy radiated may be considerable and may ruin radio reception over a large area. This radiated energy may be strongest at the natural frequency of the radiating wires but, because of the high resistance of the spark gap, the disturbance may cover a very wide band of frequencies.

Condensers across the place where the spark occurs reduce both spark and interference; inductances in series with the power wires leading to the electrical machine creating the disturbance prevent the radiations from getting into the power lines and hence from having much of a radiating system. Combinations of inductances and condensers may filter out the radiations by reducing or preventing sparks, by shunting them into the ground and by preventing them from getting into power lines (Fig. 306).

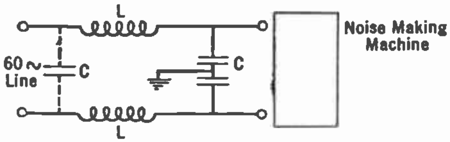


Fig. 306.—Use of noise "filter."

To tell whether noise in a receiver comes from outside or from the receiver or power equipment itself it is only necessary to disconnect the antenna. If the noise persists, its origin is within the receiver or power supply. If it is reduced, it is being picked up by the antenna. A directional receiver may be used to determine first its general direction and finally its exact location. Noise in " a.c. operated " or electric sets may come in over the power wires and then it will be heard even though the antenna is disconnected.

The complete elimination of interference from true static and from man-made radio disturbances is one of the few big radio problems that have not yet been solved.

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D

E

F

Relation between Wave Length in Meters, Frequency in Kilocycles, and the Product of Inductance (in Microhenries) and Capacity (in Microfarads)

Meters	*f* in Kc.	L×C	Meters	*f* in Kc.	L×C	Meters	*f* in Kc.	L×C
1	300,000	0.0000003	450	667	0.0570	740	405	0.1541
2	150,000	0.0000111	460	652	0.0596	745	403	0.1562
3	100,000	0.0000018	470	639	0.0622	750	400	0.1583
4	75,000	0.0000045	480	625	0.0649	755	397	0.1604
5	60,000	0.0000057	490	612	0.0676	760	395	0.1626
6	50,000	0.0000101	500	600	0.0704	765	392	0.1647
7	42,900	0.0000138	505	594	0.0718	770	390	0.1669
8	37,500	0.0000180	510	588	0.0732	775	387	0.1690
9	33,333	0.0000228	515	583	0.0747	780	385	0.1712
10	30,000	0.0000282	520	577	0.0761	785	382	0.1734
20	15,000	0.0001129	525	572	0.0776	790	380	0.1756
30	10,000	0.0002530	530	566	0.0791	795	377	0.1779
40	7,500	0.0004500	535	561	0.0806	800	375	0.1801
50	6,000	0.0007040	540	556	0.0821	805	373	0.1824
60	5,000	0.0010140	545	551	0.0836	810	370	0.1847
70	4,290	0.0013780	550	546	0.0852	815	368	0.1870
80	3,750	0.0018010	555	541	0.0867	820	366	0.1893
90	3,333	0.0022800	560	536	0.0883	825	364	0.1916
100	3,000	0.00282	565	531	0.0899	830	361	0.1939
110	2,727	0.00341	570	527	0.0915	835	359	0.1962
120	2,500	0.00405	575	522	0.0931	840	357	0.1986
130	2,308	0.00476	580	517	0.0947	845	355	0.201
140	2,143	0.00552	585	513	0.0963	850	353	0.203
150	2,000	0.00633	590	509	0.0980	855	351	0.206
160	1,875	0.00721	595	504	0.0996	860	349	0.208
170	1,764	0.00813	600	500	0.1013	865	347	0.211
180	1,667	0.00912	605	496	0.1030	870	345	0.213
190	1,579	0.01015	610	492	0.1047	875	343	0.216
200	1,500	0.01126	615	488	0.1065	880	341	0.218
210	1,429	0.01241	620	484	0.1082	885	339	0.220
220	1,364	0.01362	625	480	0.1100	890	337	0.223
230	1,304	0.01489	630	476	0.1117	895	335	0.225
240	1,250	0.01621	635	472	0.1135	900	333	0.228
250	1,200	0.01759	640	469	0.1153	905	331	0.231
260	1,154	0.01903	645	465	0.1171	910	330	0.233
270	1,111	0.0205	650	462	0.1189	915	328	0.236
280	1,071	0.0221	655	458	0.1208	920	326	0.238
290	1,034	0.0237	660	455	0.1226	925	324	0.241
300	1,000	0.0253	665	451	0.1245	930	323	0.243
310	968	0.0270	670	448	0.1264	935	321	0.246
320	938	0.0288	675	444	0.1283	940	319	0.249
330	909	0.0306	680	441	0.1302	945	317	0.251
340	883	0.0325	685	438	0.1321	950	316	0.254
350	857	0.0345	690	435	0.1340	955	314	0.257
360	834	0.0365	695	432	0.1360	960	313	0.259
370	811	0.0385	700	429	0.1379	965	311	0.262
380	790	0.0406	705	426	0.1399	970	309	0.265
390	769	0.0428	710	423	0.1419	975	308	0.268
400	750	0.0450	715	420	0.1439	980	306	0.270
410	732	0.0473	720	417	0.1459	985	305	0.273
420	715	0.0496	725	414	0.1479	990	303	0.276
430	698	0.0520	730	411	0.1500	995	302	0.279
440	682	0.0545	735	408	0.1521			

AVERAGE CHARACTERISTICS OF RECEIVING VACUUM TUBES

Detectors and Amplifiers

GENERAL								DETECTION			AMPLIFICATION									
Type	Use	Base	Maximum Over-all Dimensions, Inches: Height	Maximum Over-all Dimensions, Inches: Diameter	Filament Supply	Filament Terminal, Volts	Filament Current, Amperes	Plate Supply, Volts	Plate Current, Milliamperes	Grid Return Lead To	Plate Supply, Volts	Grid Bias Voltage on Filament: D.C.	Grid Bias Voltage on Filament: A.C.	Plate Current, Milliamperes	Screen Grid, Volts	A. C. Plate Resistance, Ohms	Mutual Conductance, Micromhos	Voltage Amplification Factor	Ohms Load for Maximum Undistorted Output	Maximum Undistorted Output, Milliwatts
11	Detector or Amplifier	WD-11	4⅛	1 3/16	D. C.	1.1	0.25	45	1.5	+F	90 135	4.5 10.5	....	2.5 3.0	....	15,500 15,000	425 440	6.6 6.6	15,500 18,000	7 35
12	Detector or Amplifier	UX	4 11/16	1 3/16	D. C.	1.1	0.25	45	1.5	+F	90 135	4.5 10.5	....	2.5 3.5	....	15,500 15,000	425 440	6.6 6.6	15, 18,000	7 35
112-A	Detector or Amplifier	UX	4 11/16	1 13/16	D. C.	5.0	0.25	45	4.0	+F	90 135	4.5 9.0	....	5.2 6.2	....	5,600 5,300	1500 1600	8.5 8.5	5,600 8,700	30 120
199	Detector or Amplifier	UV-199	3½	1 3/16	D. C.	3.3	0.063	45	1.0	+F	90	4.5	......	2.5	......	15,500	425	6.6	15,500	7
199	Detector or Amplifier	Small UX	4¼	1 3/16	D. C.	3.3	0.063	45	1.0	+F	90	4.5	......	2.5	......	15,500	425	6.6	15,500	7
200-A	Detector	UX	4 11/16	1 13/16	D. C.	5.0	0.25	45	1.5	−F	Following UX-200-A Characteristics Apply Only for Detector Connection					30,000	666	20.0		
201-A	Detector or Amplifier	UX	4 11/16	1 13/16	D. C.	5.0	0.25	45	1.5	+F	90 135	4.5 9.0	....	2.5 3.0	....	11,000 10,000	725 800	8.0 8.0	11,000 20,000	15 55
222	Radio Freq. Amplifier	UX	5⅝	1 13/16	D. C.	3.3	0.132	.....	.....	.....	135 135	1.5 1.5	....	1.5 3.3	45.0 67.5	850,000 600,000	350 480	300.0 290.0		
222	Audio Freq. Amplifier	UX	5⅝	1 13/16	D. C.	3.3	0.132	.....	.....	.....	180*	1.5	......	0.3	22.5	2,000,000	175	350.0		
224	Radio Freq. Amplifier or Detector	UY	5¼	1 13/16	A. C. or D. C.	2.5	1.75	Refer to Technical Bulletin		Cath.	180 180	1.5 3.0	1.5 3.0	4.0 4.0	75.0 90.0	400,000 400,000	1050 1000	420.0 400.0		
224	Audio Freq. Amplifier	UY	5¼	1 13/16	A.C. or D.C.	2.5	1.75	.....	.....	.....	250†	1.0	1.0	0.5	25.0	2,000,000	500	1000.0		
226	Amplifier	UX	4 11/16	1 13/16	A. C. or D. C.	1.5	1.05	.....	.....	.....	90 135 180	5.0 8.0 12.5	6.0 9.0 13.5	3.8 6.3 7.4	....	8,600 7,200 7,000	955 1135 1170	.2 8.2	9,800 8,800 10,500	30 80 180
227	Detector or Amplifier	UY	4 11/16	1 13/16	A. C. or D. C.	2.5	1.75	45	3.5	Cath.	90 135 180	6.0 9.0 13.5	6.0 9.0 13.5	2.7 4.5 5.0	....	11,000 9,000 9,000	820 1000 1000	9.0 9 0 9 0	14,000 13,000 18,700	30 80 165
230	Detector or Amplifier	Small UX	4¼	1 3/16	D. C.	2.0	0.06	45	1.0	+F	90	4.5	......	2.0	......	12,500	700	8.8		
232	Radio Freq. Amplifier	UX	5¼	1 13/16	D. C.	2.0	0.06	.....	.....	.....	135	3.0	......	1.5	67.5	800,000	550	440.0		
‡235	Radio Freq. Amplifier	UY	5¼	1 13/16	A.C. or D.C.	2.5	1.75	.....	.....	.....	180 250	1.5 3.0	1.5 3.0	6.0 7.0	75.0 90.0	250,000 300,000	1100 1000	5.0 300.0		
‡236	R. F. Amp. or Detector	UY	4 11/16	1 3/16	D. C.	6.3	0.3	.....	.....	.....	90 135	1.5 1.5	....	1.8 3.5	55.0 75.0	200,000 250,000	850 1100	170.0 275.0		
‡237	Detector or Amplifier	UY	4¼	1 3/16	D. C.	6.3	0.3	.....	.....	.....	90 135	6.0 9.0	....	2.7 4.5	....	11,500 10,000	780 900	9.0 9.0	14,000 12,500	30 75
240	Detector or Amplifier	UX	4 11/16	1 13/16	D. C.	5.0	0.25	135* 180*	0.3 0.4	+F	135* 180*	1.5 3.0	....	0.2 0.2	....	150,000 150,000	200 200	30.0		
112-A	Power Amplifier	UX	4 11/16	1 13/16	D. C. or A.C.	5.0	0.25	.....	.....	.....	135 180	9.0 13.5	11.5 15.0	6.2 7.6	....	5,300 5,000	1600 1700	8.5	8,700 10,800	120 260
120	Power Amplifier	Small UX	4¼	1 3/16	D. C.	3.3	0.132	.....	.....	.....	135	22.5	......	6.5	......	6,300	525	3.3	6,500	
		UX	4 11/16	1 13/16	or D. C.	5.0	0.25	....	.....	.....					......					
				2 3/16	A. C. or	7.5	1.25	.....	.....	.....	.0 .0	22. 31.0 39.0		.0 0	......		1		11,	
										......	135	22.5	......		.....	4,000	875	5	....	170
																45,000				
										....	135	13.5	...				900			
							5	..	.....	.....					.....	1,				
		UY	5⅝	2 3/16	A. C.	2.5	1.5	.....	.....	.....	250	15.0	16.5	32.0	.0	38,000	2500	95.0		
		UX	6¼	2 11/16	C. or or D. C.	7.5	1.25	.....	.....	.....	250 350 400 450	41.0 59.0 66.0 80.0	63.0 70.0 84.0	.0 0 0	....	2,100 1, 1 1	1 2000 2100 2100			
280	Full-Wave Rectifier	UX	5⅝	2 3/16	A. C.	5.0	2.0	1. D. C. per te Current (Maximum ....125 to filter 2. A. C. V per Plate (Maximum RMS.).......400 refer to D. C. Output Current (Maximum MA. 110												
281	W Rectifier	UX	6¼	2 3/16	A. C.	7.5	1.25	Voltage V).......... D. C. Output Current (Maximum MA.)............... 85 to filter of												
874	Voltage Regulator	UX	5⅝	2 3/16				Designed to keep output voltage of B-Eliminators constant when different values of "B" current are supplied.											 1	
876	Regulator (Ballast	Mogul	8	2 3/16				Designed to insure constant input to power-operated radio receivers despite fluctuations in line voltage.										Operating Current..... 1.7 Amperes Voltage Range........ 40–60 Volts		
886		Mogul	8	2 3/16				Designed to insure constant input to power-operated radio receivers despite fluctuations in line voltage.										Operating Current..... 2.05 Amperes Voltage Range........ 40–60 Volts		

FOR AMATEUR AND EXPERIMENTAL TRANSMITTING USE

Type	Use	Base	Maximum Over-all Dimensions, Inches: Height	Maximum Over-all Dimensions, Inches: Weight	Filament Terminal, Volts	Filament Current, Amperes	Voltage Amplification Factor	Normal Plate, Volts	Approximate Grid Bias, Volts	Approximate Screen, Volts	Maximum Plate	Maximum Plate Dissipation, Watts	N
852	F or	UX	8¾	6⅜	10.0	3.25	12		250	....	.	100	75.0
			6¼	2 3/16	7.5	2.	1			125			7.5
866		UX	6⅜	2 3/16	2.5	5.0			V	......	.6 15		

* Applied through plate of ohms. † through